

december 1958
the
institute
of
radio
engineers

Proceedings of the IRE

in this issue

NONLINEAR RESISTIVE ELEMENTS

RADIO SYSTEM PERFORMANCE IN NOISE

GAIN-BANDWIDTH OF TRANSISTORS

IRE STANDARDS ON AUDIO TERMS

SHORT-WAVE FREQUENCY VARIATIONS

IRE STANDARDS ON RECORD CALIBRATION

TRANSACTIONS ABSTRACTS

ABSTRACTS AND REFERENCES

PROCEEDINGS INDEX

NATIONAL CONVENTION RECORD INDEX

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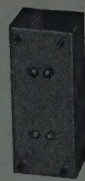
400 — telemetering, 3 db at $\pm 7.5\%$, 40 db at 230 and 700 — $\frac{1}{2} \times 1\frac{1}{4} \times 2\frac{1}{2}$.



15 — BP filter, 20 db at 30 — 45 db at 100 — phase angle at CF less than 3° from -40 to $+100^\circ$ C.



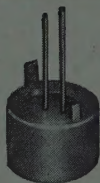
LP filter within 1 db to 49 KC, stable to .1 db from 0 to 85° C., 45 db at 55 KC.



LP filter less than .1 db 0 to 2.5 KC, 50 db beyond 3 KC.



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HVC tapped variable inductor for 3 KC oscillator.

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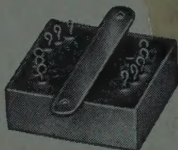
Toroid, laminated, and cup structures from .1 cycle to 400 MC.

SPECIALTIES

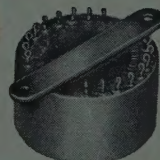
Saturable reactors, reference transformers, magnetic amplifiers, combined units.



RF saturable inductor for sweep from 17 MC to 21 MC.



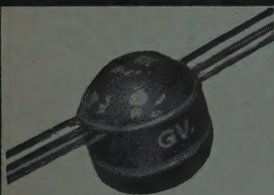
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December, 1958*published monthly by The Institute of Radio Engineers, Inc.***Proceedings of the IRE** [®]*contents*

Poles and Zeros	1907
E. H. Schulz, Director, 1958-1959	1908
Scanning the Issue	1909

PAPERS	General Power Relationships for Positive and Negative Nonlinear Resistive Elements, <i>Richard H. Pantell</i>	1910
	Correction to "Error Probabilities for Binary Symmetric Ideal Reception through Nonselective Slow Fading and Noise," <i>G. L. Turin</i>	1913
	Performance of Some Radio Systems in the Presence of Thermal and Atmospheric Noise, <i>A. D. Watt, R. M. Coon, E. L. Maxwell, and R. W. Plush</i>	1914
	Structure-Determined Gain-Band Product of Junction Triode Transistors, <i>J. M. Early</i>	1924
	IRE Standards on Audio Techniques: Definitions of Terms, 1958	1928
	Frequency Variations in Short-Wave Propagation, <i>Toru Ogawa</i>	1934
	IRE Standards on Recording and Reproducing: Methods of Calibration of Mechanically- Recorded Lateral Frequency Records, 1958	1940
CORRESPONDENCE	D-Day in Engineering Education, <i>C. E. Hendrix and G. W. Hann</i>	1947
	Current Build-Up in Semiconductor Devices, <i>W. Shockley and J. Gibbons</i>	1947
	On the Need for Revision in Transistor Terminology and Notation, <i>H. L. Armstrong</i>	1949
	Antipodal Reception of Sputnik III, <i>O. K. Garriott and O. G. Villard, Jr.</i>	1950
	WWV Standard Frequency Transmissions, <i>W. D. George</i>	1950
	Compound Interferometers, <i>N. F. Barber, A. E. Covington, and N. W. Broten</i>	1951
	Potential Well Theory of Velocity Modulation, <i>Louis Gold</i>	1952
	Parallel Plane Waveguide Partially Filled with a Dielectric, <i>M. Cohn</i>	1952
	An Effect of Pulse Type Radiation on Transistors Packaged in a Moist Atmosphere, <i>W. A. Bohan, M. G. Chasanov, E. N. Schroeder</i>	1953
	Theory of the P-N Junction Device Using Avalanche Multiplication, <i>Toshio Misawa</i>	1954
	Number of Trees in a Graph, <i>Louis Weinberg</i>	1954
	Algebraic Approach to Signal Flow Graphs, <i>Amos Nathan</i>	1955
	On the Coupling Coefficients in the "Coupled-Mode" Theory, <i>Amnon Yariv</i>	1956
	Effect of Beam Coupling Coefficient on Broad-Band Operation of Multicavity Klystrons, <i>S. V. Yadavalli</i>	1957
	Improvements in Some Bounds on Transient Responses, <i>Armen H. Zemanian</i>	1958
	Geometric-Analytic Theory of Noisy Two-Port Networks, <i>E. Folke Bolinder</i>	1959
	Comparison of Phase Difference and Doppler Shift Measurements for Studying Ionospheric Fine Structure Using Earth Satellites, <i>M. C. Thompson, Jr., and D. M. Waters</i>	1960
	AM Transmitters As SSB Jammers, <i>John P. Costas</i>	1960
	Taper Sections in Circular Waveguides, <i>Giorgio Gerosa</i>	1961
	Common Emitter Transistor Amplifiers, <i>R. F. Purton</i>	1961
	Resonance-Probability and Entropy-Evolution Relationships, <i>George H. Amber</i>	1962
	The Dependence of Minority Carrier Lifetime on Majority Carrier Density, <i>D. M. Evans</i>	1962
	The Internal Current Gain of Drift Transistors, <i>F. J. Hyde</i>	1963
	Theory of Diode and Transistor Noise, <i>H. F. Mataré</i>	1964
	Dispersion of High-Frequency Elastic Waves in Thin Plates, <i>David L. Arenberg</i>	1965
	Computer Fabrication and Circuit Techniques, <i>Fred Herzfeld</i>	1965
	Radiometer Circuits, <i>Martin Graham</i>	1966
	Application of Inductive Probability to Communications, <i>Leonard S. Schwartz</i>	1966
	A Transistor-Magnetic Core Binary Counter, <i>Henry R. Irons</i>	1967
	Tropospheric Effects on 6-MC Pulses, <i>Richard Silberstein</i>	1968

Proceedings of the IRE[®]

continued

A New Type of Fading Observable on High-Frequency Radio Transmissions Propagated over Paths Crossing the Magnetic Equator, <i>K. C. Yeh and O. G. Villard, Jr.</i>	1968
A Note Concerning Instantaneous Frequency, <i>D. A. Linden</i>	1970

REVIEWS Scanning the TRANSACTIONS	1972
--	------

Books:

"Feedback Theory and its Applications," by P. H. Hammond, <i>Reviewed by John E. Bertram</i>	1973
"Space Charge Waves and Slow Electromagnetic Waves," by A. H. W. Beck, <i>Reviewed by J. R. Pierce</i>	1973
"English-Russian, Russian-English Electronics Dictionary," compiled by Department of the Army, <i>Reviewed by Paul E. Green, Jr.</i>	1974
"Magnetic Tape Recording," by H. G. M. Spratt, <i>Reviewed by A. Meyerhoff and K. McIlwain</i>	1974
"Television Engineering, Vol. IV: General Circuit Techniques," by S. W. Amos and D. C. Birkinshaw, <i>Reviewed by E. T. Jaynes</i>	1974

Recent Books	1975
--------------------	------

ABSTRACTS Abstracts of IRE TRANSACTIONS	1975
Abstracts and References	1980

INDEXES 1958 PROCEEDINGS OF THE IRE INDEX	Follows page 1994
1958 IRE NATIONAL CONVENTION RECORD INDEX	Follows page 1994
1958 IRE WESCON CONVENTION INDEX	Follows page 1994

IRE NEWS AND NOTES Calendar of Coming Events	14A
Available IRE Standards	15A

DEPARTMENTS Contributors	1971
IRE People	30A
Industrial Engineering Notes	64A
Meetings with Exhibits	8A
Membership	70A
News-New Products	22A
Positions Open	134A
Positions Wanted by Armed Forces Veterans	130A
Professional Group Meetings	60A
Section Meetings	78A
Advertising Index	177A

COVER Unusual interference patterns can be produced by reflecting colored light from the grooves of a revolving phonograph record modulated at a single frequency. By measuring the distance between certain of the irregular dark lines that run upward through the white lines, the modulation amplitude of the grooves can be calculated, as described in the IRE Standards on page 1940.

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Airborne Instruments Laboratory Monograph on page 4A.

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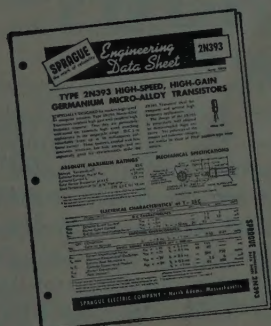
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This monograph is the second of a series in which Warren White expands on the general analogy between gravitational and electromagnetic fields.

Electromagnetic Analogues For Gravity (Part 2)

Last month, we discussed the fact that Newton's law of universal gravitation and Coulomb's law could be combined in a single unified expression. This expression which gives the static force between two particles is

$$F = \text{Re} \left\{ k \frac{s_1 s_2}{d^2} \right\}.$$

It will be remembered that s is a complex quantity representing the substance of a particle and that the real part of substance is mass while the imaginary part is charge.

We also discussed the Coriolis force which acts on a moving mass in the same manner as a magnetic field acts on a moving charge. In vector notation, the Coriolis force is given by

$$\mathbf{F} = m 2\boldsymbol{\omega} \times \mathbf{v}$$

while the magnetic force on a moving charge is of course,

$$\mathbf{F} = q \mathbf{v} \times \mathbf{B} = -q \mathbf{B} \times \mathbf{v}$$

These two expressions are naturally combined in the unified expression

$$\mathbf{F} = \text{Re} [s \mathbf{C} \times \mathbf{v}]$$

In this expression, \mathbf{C} is a vector field with complex components. We call \mathbf{C} the centrifuge field. The name is suggested by the fact that the Coriolis or real part of the centrifuge field is generated by the universe centrifuging relative to our coordinate system while the imaginary part or the magnetic field is normally generated by electrons centrifuging either in the wires of a solenoid coil or in molecular orbits.

As in the case of the Coulomb-Newton law, we have a choice of units that may be used. Assuming that in any case we measure length in centimeters and time in seconds, we may measure substance in abcoulombs and centrifuge field in gauss. Alternatively, we may measure substance in grams and centrifuge field in units corresponding to a rotation of one half radian per

second. Henceforth this last unit will be called the radian unit. Since one gram of substance is equal to 0.86×10^{-14} abcoulombs, we conclude that one gauss is equal to 0.86×10^{-14} radian units or that one radian unit is equal to 1.16×10^{-14} gauss.

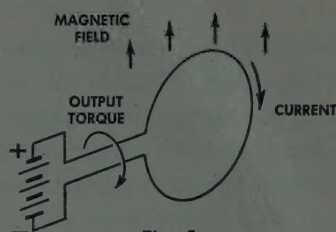


Fig. 1

Single Turn Current Loop
in Magnetic Field

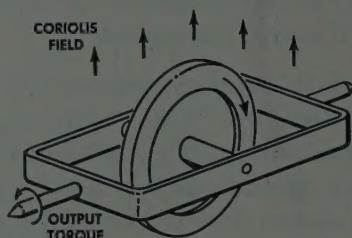


Fig. 2

Gyro in Coriolis Field

Figs. 1 & 2 illustrate the analogy between a spinning gyro rotor and a single turn loop of wire carrying current. If the loop of wire is submerged in a uniform magnetic field, it will experience a torque which is given by the expression

$$T = iAB \sin \phi$$

where i is the current flowing in the loop, A is the area of the loop, B is the magnetic field, and ϕ is the angle between the direction of the field and the normal to the plane of the loop. The unified expression which covers

both the case of the gyro rotor and the current loop is by analogy

$$T = \text{Re} [fAC \sin \phi]$$

In this expression, f is the substance flow. In the case of the gyro rotor of mass m spinning with an angular velocity Ω , f is given by the expression

$$f = m \frac{\Omega}{2\pi}$$

The expression for gyro torque assumes a more familiar form if we substitute this value for f and in addition, make the substitutions

$$A = \pi R^2$$

$$C = 2\omega$$

The expression for torque then becomes

$$T = m R^2 \Omega \omega \sin \phi$$

$$T = L \omega \sin \phi$$

where

$L = I \Omega$ is the angular momentum

$I = m R^2$ is the moment of inertia

This is the standard formula to be found in most textbooks. It may be noted in passing that L , the angular momentum, is analogous to $2iA$ or twice the magnetic dipole moment of the current loop. We may think of it as being equivalent to a Coriolis dipole moment.

Thus far, our analogy has not departed from the laws of classical physics. The unified formulas we have written are not new statements of fact but are merely restatements of the old laws in a different form. Next month we will conclude this series with a discussion of induced Coriolis fields. In postulating the existence of such fields, the electromagnetic analogy goes beyond the bounds of classical physics although it is still in harmony with the general theory of relativity.

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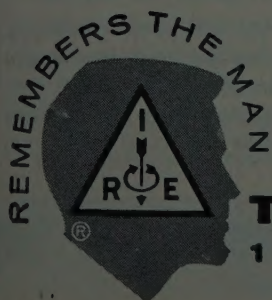
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Meetings with Exhibits



● As a service both to Members and the industry, we will endeavor to record in this column each month those meetings of IRE, its sections and professional groups which include exhibits.

Δ

December 9-11, 1959

Mid-America Electronics Convention,
Municipal Auditorium, Kansas City, Mo.

Exhibits: Mr. Leo Schlesselman, Bendix Aviation Corp., Box 1159, Kansas City, 41, Mo.

March 3-5, 1959

Western Joint Computer Conference,
Fairmont Hotel, San Francisco, Calif.

Exhibits: Mr. H. K. Farrar, Pacific Tel. & Tel. Co., 140 New Montgomery St., San Francisco 5, Calif.

March 23-26, 1959

Radio Engineering Show and National IRE Convention, New York Coliseum and Waldorf-Astoria Hotel, New York, N.Y.

Exhibits: Mr. William C. Copp, Institute of Radio Engineers, 72 West 45th St., New York 36, N.Y.

April 5-10, 1959

Fifth Nuclear Congress, Cleveland, Ohio.

Exhibits: Dr. John C. Simons, Jr., National Research Corp., 70 Memorial Drive, Cambridge 42, Mass.

April 16-18, 1959

SWIRECO, Southwestern IRE Regional Conference & Electronics Show, Dallas Memorial Auditorium & Baker Hotel, Dallas, Tex.

Exhibits: Mr. John McNeely, Southwestern Bell Telephone Co., 308 South Akard St., Dallas 1, Tex.

May 4-6, 1959

National Aeronautical Electronics Conference, Dayton Biltmore Hotel, Dayton, Ohio.

Exhibits: Mr. Edward M. Lisowski, General Precision Lab., Inc., Suite 452, 333 West First St., Dayton 2, Ohio

May 6-8, 1959

Seventh Regional Technical Conference and Trade Show, University of New Mexico, Albuquerque, N.M.

Exhibits: Mr. H. S. Wescott, Jr., Hoover Electronics Co., 1122 C. San Mateo, S.E., Albuquerque, N.M.

June 3-5, 1959

Armed Forces Communications & Electronics Association Convention & Exhibit, Sheraton-Park Hotel, Washington, D.C.

Exhibits: Mr. William C. Copp, 72 West 45th St., New York 36, N.Y.

June 4-5, 1959

Third National Conference on Production Techniques, Villa Hotel, San Mateo, Calif.

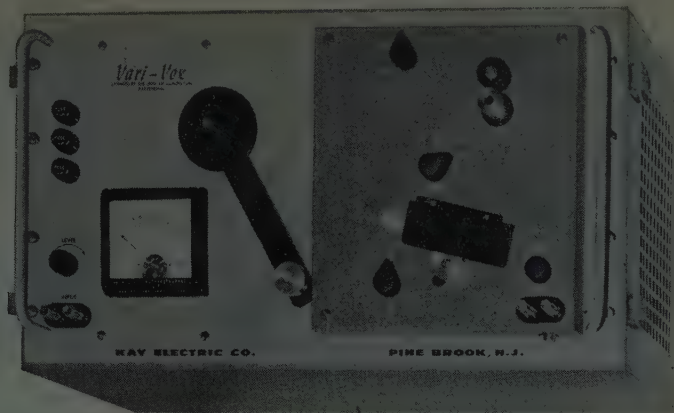
Exhibits: Mr. Estrada Fanjul, Stanford Research Institute, Menlo Park, Calif.

(Continued on page 10A)

NEW!

KAY *Vari-Vox*

CATALOG NO. 615-A



SPEEDS SPEECH TO TWICE NORMAL RATE ... or SLOWS SPEECH TO HALF NORMAL RATE

and Still Retains Intelligibility

DOUBLES INFORMATION TRANSMITTED FOR SAME TIME AND BANDWIDTH

The Kay *Vari-Vox* is a speech-time compressor and expander. During expansion or compression, it repeats or discards parts of audio signals—such as vowels, consonants, pauses in speech—and retransmits the complex signal so that complete intelligibility is retained.

Intelligence fed into the *Vari-Vox* may be speeded up and then compressed, or slowed down and then expanded by a known factor to restore the original meaning. Information fed into the *Vari-Vox* may be transmitted at 18 different speeds between twice the original rate down to one-half the original rate. The degree of compression or expansion versus the speed of the input recording determines intelligibility.

SPECIFICATIONS

Frequency Response: 500-8,000 cps \pm 2.0 db (max).

Input Impedance: 600 ohms.

Input Signal Recommended: 0.2 V rms.

Sensitivity: 0.10 V rms for full-scale operation.

Output Impedance: 600 ohms.

Output Signal: 0.20 V rms.

Information Rate: Compression up to 2 times
normal rate in 9 steps.

Expansion down to one-half
normal rate in 9 steps.

Recording Indicator: Standard V. U. Meter.

Power Supply: Self-contained.

Power Requirements: 100 watts, 117 V (\pm 10%),
50-60 cps ac.

Dimensions: 10½" x 19" x 9" rack panel.

Weight: 45 lbs.

Price: \$1,495.00, f.o.b. factory. (Add 10% for export.)

Vari-Vox APPLICATIONS (Partial List)

Compression

- Speed up Data Read-out
- Cut Monitoring Time and Tape Storage
- Faster Analysis of Complex Signals
- Reduce Time, Material and Storage in Talking Books or Speech Records
- Increase Information Rate for Signal Monitoring
- Frequency Multiplication of Read-out Signal

Expansion

- Better Interpretation of Foreign Language Monitoring
- Stenographic Transcription of "Difficult" Subject Matter
- Phonetics and Voice Studies
- Foreign Language Studies
- Greater Intelligibility in the Presence of Noise
- Frequency Division of Read-out Signal

Write for New Kay Catalog

KAY ELECTRIC COMPANY

Dept. I-12

Maple Avenue

Pine Brook, N. J.

Capital 6-4000

B SUBMINIATURE 13-DIGIT ENCODER for airborne or other limited space applications. Detailed specifications in Bulletin 0858. **SIZE:** $2\frac{3}{16}$ " dia. \times $3\frac{3}{4}$ " long; $\frac{1}{4}$ " dia. shaft, $\frac{7}{8}$ " long. **WEIGHT:** $1\frac{1}{4}$ lbs. **OVERALL ACCURACY:** $\pm 1\frac{1}{4}$ quanta in 8192. **READOUT RATE:** Model A, nominally 10KC (50 microsecond pulse), max. of 100KC (5 microsecond pulse). Model B, max. of 200KC for element, 10KC for sequence. **MAXIMUM ANGULAR SPEED OF ROTATION AT FULL ACCURACY:** 2 rpm (6 rpm at 12-digit accuracy). 10 rpm with temperature control.

B 4" DIA. 13-DIGIT ENCODER for general purpose applications. Detailed specifications in Bulletin 0958. **SIZE:** 4" OD with protrusions on one side \times 7" long; $\frac{1}{4}$ " dia. shaft, 0.67" long. **WEIGHT:** $9\frac{1}{4}$ lbs. **OVERALL ACCURACY:** ± 1 quanta in 8192. **READOUT RATE:** 100 cps, max. **MAXIMUM ANGULAR SPEED OF ROTATION AT FULL ACCURACY:** 720 rpm; maximum rotation rate, 600 rpm.

B 6" DIA. 13-DIGIT ENCODER for general purpose applications. Specifications in Bulletin 1058. **SIZE:** $6\frac{3}{16}$ " dia. with protrusions \times $7\frac{3}{4}$ " long; $\frac{1}{2}$ " dia. shaft, 1" long. **WEIGHT:** 1 $\frac{1}{2}$ lbs. **OVERALL ACCURACY:** ± 1 quanta in 8192. **READOUT RATE:** 100 cps, max. **MAXIMUM ANGULAR SPEED OF ROTATION AT FULL ACCURACY:** 720 rpm (10 microsecond pulse).



Model A2ESS13
(Parallel readout)
Model B2ESS13
(Sequential readout)



Model A4DP13



Model A6DP13

Now from Baldwin® precision shaft angle analog-to-digital encoders in 5 standard models:

13, 16 and 18 digit /
photoelectric readout / reflected binary code*.

B 9" DIA. 16-DIGIT ENCODER precision unit for radar applications. Detailed specifications in Bulletin 1158. **SIZE:** $9\frac{1}{16}$ " dia. with protrusions \times $4\frac{3}{8}$ " high; $\frac{1}{2}$ " dia. shaft, $1\frac{1}{4}$ " long. **WEIGHT:** $17\frac{1}{2}$ lbs. **OVERALL ACCURACY:** ± 1 quanta in 65,536. **READOUT RATE:** 100 cps, max. **MAXIMUM ANGULAR SPEED OF ROTATION AT FULL ACCURACY:** 90 rpm (10 microsecond pulse)



Model A9SP16

B HIGH PRECISION 18-DIGIT ENCODER for radar or theodolite applications. Detailed specifications in Bulletin 1258. **SIZE:** 21" max. dia. \times $8\frac{1}{16}$ " high. **WEIGHT:** 169 lbs. **OVERALL ACCURACY:** ± 1 quanta in 262,144. **READOUT RATE:** 100 cps, max. **MAXIMUM ANGULAR SPEED OF ROTATION AT FULL ACCURACY:** 25 rpm (10 microsecond pulse).



Model A2TSP18

*Encoders with decimal, trigonometric functions and other nonlinear codes are also available. All disks are made on a special divided circle machine designed and built by Baldwin. Write for descriptive bulletins.

Industrial Products Division

THE BALDWIN PIANO COMPANY

1803 Gilbert Avenue, Cincinnati 2, Ohio

Meetings with Exhibits

(Continued from page 8A)

June 13-22, 1959

International Conference on Information Processing, UNESCO House & Palais d'Exhibition, Paris, France.

Exhibits: Mr. E. M. Grabbe, Ramo Wooldridge Corp., Box 45067, Airport Station, Los Angeles 45, Calif.

June 29-July 1, 1959

Third National Convention on Military Electronics, Sheraton-Park Hotel, Washington, D.C.

Exhibits: Mr. L. David Whitelock, Bu-Ships, Electronics Div., Dept. of Navy, Washington, D.C.

August 18-21, 1959

WESCON, Western Electronic Show and Convention, Cow Palace, San Francisco, Calif.

Exhibits: Mr. Don Larson, WESCON, 1435 La Cienega Blvd., Los Angeles, Calif.

October 7-9, 1959

IRE Canadian Convention, Exhibition Park, Toronto, Ont., Canada.

Exhibits: Mr. F. G. Heath, IRE Canadian Convention, 1819 Yonge St., Toronto 7, Ont., Canada.

October 12-15, 1959

National Electronics Conference, Hotel Sherman, Chicago, Ill.

Exhibits: Mr. Brendon C. Hawkins, National Electronics Conference, Inc., 184 E. Randolph St., Chicago 1, Ill.

October 26-28, 1959

East Coast Aeronautical & Navigational Electronics Conference, Lord Baltimore Hotel & 7th Regiment Armory, Baltimore, Md.

Exhibits: Mr. R. L. Pigeon, Westinghouse Electric Corp., Air Arm Div., P.O. Box 746, Baltimore, Md.

November 9-11, 1959

Fourth Instrumentation Conference, Atlanta, Ga.

Exhibits: Dr. B. J. Dasher, School of E.E., Georgia Institute of Technology, Atlanta 13, Ga.

November 30-December 3, 1959

Eastern Joint Computer Conference, Hotel Statler, Boston, Mass.

Exhibits: Mr. John M. Broomall, Burroughs Corporation, Paoli, Pa.

Note on Professional Group Meetings: Some of the Professional Groups conduct meetings at which there are exhibits. Working committeemen on these groups are asked to send advance data to this column for publicity information. You may address these notices to the Advertising Department and of course listings are free to IRE Professional Groups.

PERKIN

FOR THE FIRST TIME... 28V AT 100 AMPERE
transistorized, virtually transient-free
DC POWER SUPPLY

A MAJOR BREAK THROUGH IN DC POWER!!

Realizing a definite need for dynamically regulated D.C. Power in high current capacities, Perkin Engineering has pioneered the development of a line of units headed by 100 ampere, completely transistorized, power supply, with excellent transient regulation which is a "must" when powering voltage sensitive equipment such as transistorized inverters, converters, etc. This unit suppresses line and load transients to a very low level virtually eliminating voltage "overshoot" and "undershoot" common with more conventional supplies.



MODEL MTR28-100

UNIQUE FEATURES OF MODEL MTR28-100

- COMPLETELY TRANSISTORIZED
- EXCELLENT DYNAMIC (TRANSIENT) REGULATION
- LOW RIPPLE
- SHORT CIRCUIT PROOF
- AUTOMATIC CURRENT LIMITING
- SILICON POWER RECTIFIERS
- FAST RESPONSE TIME
- REMOTE SENSING
- SILICON ZENER DIODE REFERENCE ELEMENT



MODEL MTR060-5



MODEL MTR28-10

SPECIFICATIONS ON MTR28-100

AC INPUT: 208/230 OR 460 V. $\pm 10\%$
3 PHASE, 60 CPS
D.C. OUTPUT: 24-32 V @ 100 A
REGULATION:
STATIC: $\pm 0.1\%$ LINE, $\pm 0.1\%$ LOAD
DYNAMIC: $\pm 0.5\%$ LINE, ± 2 V. LOAD
RIPPLE: 20 MV RMS MAX.
DYNAMIC IMPEDANCE: 0.025 OHMS MAX.
RESPONSE TIME: 1 MILLISECOND MAX.

OTHER UNITS AVAILABLE WITH COMPARABLE SPECIFICATIONS

MODEL NO.	D. C. OUTPUT VOLTS	AMPS
MTR060-1	0-60	1
MTR060-5	0-60	5
MTR636-15	6-36	15
MTR636-30	6-36	30
MTR28-2	24-32	2
MTR28-10	24-32	10
MTR28-30	24-32	30

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PERKIN

SPACE TECHNOLOGY LABORATORIES, INC.

Space Technology Laboratories, Inc., previously a division of The Ramo-Wooldridge Corporation, became a separate company on October 31, 1958. Space Technology Laboratories will be directed by Lieut. Gen. James H. Doolittle, Chairman of the Board (after January 1, 1959); Dr. Louis G. Dunn, President; and Dr. Ruben F. Mettler, Executive Vice President. The other members of the Board of Directors are Robert F. Bacher, Head of the Division of Physics, Mathematics and Astronomy at the California Institute of Technology; James T. Brown, Vice President of the Mellon National Bank, Pittsburgh, Pennsylvania; and Samuel E. Gates, Attorney with the New York firm of Debevoise, Plimpton and McLean.

Space Technology Laboratories has the largest professional scientific and engineering staff in the nation devoted exclusively to Ballistic Missile and Space programs. STL is responsible for the systems engineering and technical direction of the Air Force THOR, ATLAS, TITAN, and MINUTEMAN ballistic missile programs. While it does not engage in production, STL performs experimental and analytical research projects in advanced space technology, including the fabrication and assembly of special equipment and the conduct of test programs. A recent example is the lunar probe project assigned to STL by the Air Force and the National Aeronautics and Space Administration.

Space Technology Laboratories, Inc., plans to maintain a combination of technical competence and organizational strength appropriate to its special and continuing role in the important national program of space weapons development.

SPACE TECHNOLOGY LABORATORIES, INC.

5730 Arbor Vitae Street
Los Angeles 45, California

Thompson Ramo Wooldridge Inc.

On October 31, 1958, **Thompson Ramo Wooldridge Inc.** was formed by the merger of *Thompson Products, Inc.*, and *The Ramo-Wooldridge Corporation*.

Thompson Ramo Wooldridge will be directed by J. D. Wright, Chairman of the Board; Dean E. Wooldridge, President; Simon Ramo, Executive Vice President; and F. C. Crawford, Chairman of the Executive Committee. The other members of the Board of Directors are B. W. Chidlaw, A. T. Colwell, J. H. Coolidge, H. L. George, R. P. Johnson, and H. A. Shepard. Each is a Vice President of the merged company.

Thompson Products, Inc., has been for many years a large manufacturer of components and accessories for the automotive and aircraft industries. In recent years, it has also been active in the fields of Missiles, Electronics, and Nuclear Energy. Thompson has concentrated on products which require a high level of competence in engineering and precision manufacturing.

The Ramo-Wooldridge Corporation was organized five years ago to conduct research, development, and manufacturing operations in the field of electronic and missile systems having a high content of scientific and engineering newness. In addition to the work performed by Space Technology Laboratories, Inc., Ramo-Wooldridge has been engaged in major systems work in such areas as digital computers and control systems, communications and navigation systems, infrared systems, and electronic countermeasures.

The merger of the two companies into **Thompson Ramo Wooldridge Inc.** is intended to provide an integrated team having strong capabilities for scientific research, engineering development, and precision manufacturing.

Thompson Ramo Wooldridge Inc.

Main Offices • Cleveland 17, Ohio
Los Angeles 45, California

Calendar of Coming Events and Authors' Deadlines*

1958

Mid-Amer. Elec. Convention, Mun. Audit, Kansas City, Mo., Dec. 9-11

1959

Rel. & Qual. Control Nat'l Symp., Bellevue-Stratford Hotel, Philadelphia, Pa., Jan. 12-14

ANTEC Conf., Hotel Commodore, New York City, Jan. 27-30

Solid-State Circuits Conf., Univ. of Pa., Philadelphia, Pa., Feb. 12-13

Western Joint Computer Conf., Fairmont Hotel, San Francisco, Calif., Mar. 3-5

IRE Nat'l Convention, Coliseum and Waldorf-Astoria, New York City, Mar. 23-26

Millimeter Waves Int'l Symp., Engineering Societies Bldg., New York City, Mar. 31, Apr. 1-2

Silicon-Carbide Conf., Boston, Mass., Apr. 2-3 (DL*: Mar. 1, J. R. O'Connor, Elec. Mat'l Sci. Lab. AF Cambridge Res. Ctr., Bedford, Mass.)

Nuclear Cong., Cleveland, Ohio, Apr. 5-10

Industrial Instrumentation & Control Conf., Ill. Inst. Tech., Chicago, Ill., Apr. 14-15

SWIRECO (Southwestern Regional Conference), Dallas, Texas, Apr. 16-17 (DL*: Nov. 1, Frank Seay, Texas Instr. Inc., 6000 Lemmon Ave., Dallas 9, Tex.)

New Tech. in Instrumentation and Control, Philadelphia, Pa., Apr. 20-21

Nat'l Aero. Elec. Conf., Dayton, Ohio, May 4-6

Fifth Annual Flight Test Instr. Symp., Seattle, Wash., May 4-7

URSI Spring Meeting, Washington, D. C., May 5-7

Elec. Components Conf., Ben Franklin Hotel, Philadelphia, Pa., May 6-8

7th Reg. Tech. Conf. and Trade Show, Univ. of N. M., Albuquerque, N. M., May 6-8

Joint Conf. on Auto. Tech., Pick-Congress Hotel, Chicago, Ill., May 11-13

Internat'l Conv. on Transistors and Associated Semiconductor Devices, Earls Court, London, May 25-29

Australian IRE Radio Eng. Conv., Univ. of Melbourne, Victoria, Aus., May 25-26

Internat'l Conf. on Med. Elec., Paris, France, June

Microwave Theory & Tech., 1959 Nat'l Symp., Harvard Univ., Cambridge, Mass., June 1-3 (DL*: Jan. 15, Dr. H. J. Riblet, 92 Broad St., Wellesley, Mass.)

* DL=Deadline for submitting abstracts.

(Continued on page 15A)

SYMPOSIUM ON MILLIMETER WAVES CALLS FOR PAPERS

Millimeter waves will be the subject of the ninth international symposium of the Polytechnic Institute of Brooklyn, Microwave Research Institute, to be held in New York City on March 31, April 1, 2, 1959. Cosponsors are the Air Force Office of Scientific Research, the U. S. Army Signal Research and Development Laboratory, ONR, and the IRE. The symposium is intended to highlight the present state of research in, and applications of, millimeter wave technology. Invited and contributed papers will treat the generation, transmission, control, measurement, and detection of millimeter wave energy. In addition, source material and significant advances in basic supporting fields will be summarized in tutorial papers chosen from appropriate fields in physics and engineering.

The closing date for submission of papers and/or 100-word abstracts is January 30, 1959. All correspondence should be addressed to Professor Herbert J. Carlin, Microwave Research Institute, 55 Johnson Street, Brooklyn 1, N. Y.

A detailed indication of topics within the scope of the symposium follows.

Interaction of millimeter waves and materials—Hall effect circuits, circuits utilizing ferromagnetic and paramagnetic resonances, cryogenic circuits, ferrite devices, equivalent circuit representations for active and anisotropic structures.

Solid state active millimeter circuits—maser and parametric amplifiers and oscillators, solid state mixers and frequency multipliers, duplexing and switching circuits, active matching elements, discontinuities in active systems.

Millimeter electron tubes—oscillators and amplifiers such as klystrons, magnetrons, backward wave oscillators, etc., Cerenkov millimeter sources, relativistic electron beam harmonic generators and radiators,

millimeter-wave interaction with plasmas.

Radiating circuits and antennas—antennas for millimeter waves, equivalent circuits for radiating discontinuities, radio astronomy.

Coupled line, multimode, and nonconventional transmission systems—periodic structures in multimode waveguide, anisotropic media, surface waveguides, quasi-optic techniques, equivalent circuits for discontinuities in multimode or nonconventional waveguides.

Millimeter components—filters, transformers, directional couplers, rotary joints, quasi-optic component techniques.

Millimeter circuit measurement techniques—new measurement methods, measurement techniques for nonreciprocal and active circuits, diagnostic measurements of plasmas with millimeter waves.

IRE NATIONAL CONVENTION SET FOR MARCH 23-26

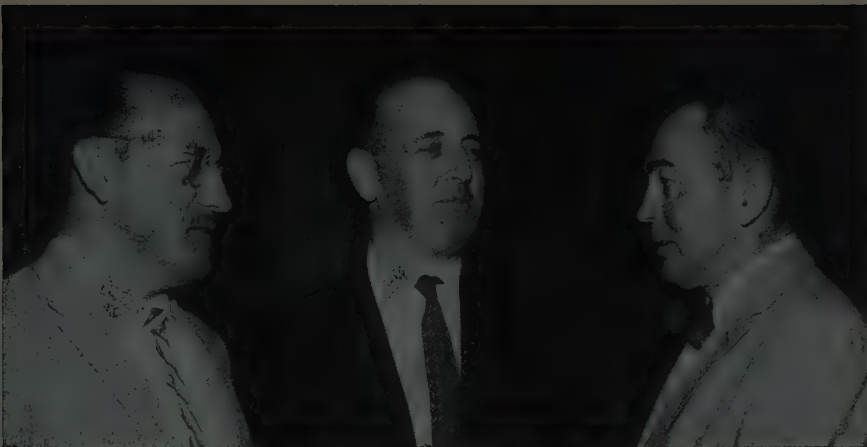
"Future Developments in Space" has been chosen as the Tuesday evening highlight session of the 1959 IRE National Convention, which will start Monday, March 23 at the Waldorf-Astoria Hotel and New York Coliseum in New York City. The four-day program of 54 sessions and 850 exhibits is expected to draw over 55,000 engineers and scientists.

The Convention will open with the IRE Annual Meeting at which Donald B. Sinclair, vice-president of the IRE for 1959, will be principal speaker.

A get-together cocktail party will be held Monday evening and the annual banquet Wednesday evening in the Waldorf's Grand Ballroom. Tickets may be purchased from IRE headquarters at \$4.50 and \$15.00, respectively. Due to the heavy attendance expected, members are urged to place their orders early.



The first annual Scott Helt Award for the best technical Broadcast Transmission Systems paper published last year was presented by Mrs. Scott Helt to J. L. Berryhill. The occasion was the Eighth Annual Broadcast Symposium, held in September in Washington, D. C. Looking on are George W. Bailey (left), Executive Secretary of the IRE, and Clure H. Owen (right), Chairman of PGBTS.



At WESCON in August, Donald G. Fink, IRE President (center), meets with L. C. Van Atta (left) and Earl Goddard (right), chairmen of the Los Angeles and San Francisco Sections, respectively. The two Sections of the IRE Seventh Region and the West Coast Electronic Manufacturers' Association cosponsored the Convention.

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IRE 2., 11., 15.S1 Standards on Antennas, Modulation Systems, and Transmitters: Definitions of Terms, 1948.....	\$0.75
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55 IRE 2.S1 Standards on Antennas and Waveguides: Definitions for Waveguide Components, 1955. Reprinted from the September, 1953, PROCEEDINGS.....	\$0.25
45 IRE 2.S2 Standards on Antennas: Methods of Testing. 1948. Adopted by ASA. (ASA C16.11-1949).....	\$0.75
54 IRE 3.S1 Standards on Audio Techniques: Definitions of Terms, 1954. Reprinted from the July, 1954, PROCEEDINGS.....	\$0.50
50 IRE 3.S1 Standards on Audio Systems and Components: Methods of Measurement of Gain, Amplification, Loss, Attenuation, and Amplitude-Frequency-Response, 1956. Adopted by ASA. (ASA C16.29-1957). Reprinted from the May, 1956, PROCEEDINGS.....	\$0.80
55 IRE 3.S1 Standards on Audio Techniques: Definitions of Terms, 1958. Reprinted from the December, 1958, PROCEEDINGS.....	\$0.60
53 IRE 3.S2 Standards on American Recommended Practice for Volume Measurements of Electrical Speech and Program Waves, 1953. Adopted by ASA. (ASA C16.5-1954). Reprinted from the May, 1954, PROCEEDINGS.....	\$0.50
50 IRE 4.S1 Standards on Circuits: Definitions of Terms in Network Topology, 1950. Reprinted from the January, 1951, PROCEEDINGS.....	\$0.50
53 IRE 4.S1 Standards on Circuits: Definitions of Terms in the Field of Linear Varying Parameter and Nonlinear Circuits, 1953. Reprinted from the March, 1954, PROCEEDINGS.....	\$0.25
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51 IRE 6.S1 Standards on Electroacoustics: Definitions of Terms, 1951. Reprinted from the May, 1951, PROCEEDINGS.....	\$1.00
52 IRE 7.S1 Standards on Magnetrans: Definitions of Terms, 1952. Reprinted from the May, 1952, PROCEEDINGS.....	\$0.25
53 IRE 7.S1 Standards on Electron Devices: Methods of Measuring Noise, 1953. Adopted by ASA. (ASA C60.13-1954). Reprinted from the July, 1953, PROCEEDINGS.....	\$0.75
54 IRE 7.S1 Standards on Electron Devices: Definitions of Terms Related to Phototubes, 1954. Reprinted from the August, 1954, PROCEEDINGS.....	\$0.25
50 IRE 7.S1 Standards on Electron Devices: Definitions of Terms, Related to Microwave Tubes (Klystrons, Magnetrons, and Traveling-Wave Tubes), 1956. Reprinted from the March, 1956, PROCEEDINGS.....	\$0.50
57 IRE 7.S1 Standards on Electron Tubes: Physical Electronics Definitions, 1957. Reprinted from the January, 1957, PROCEEDINGS.....	\$0.50
50 IRE 7.S2 Standards on Electron Tubes: Methods of Testing, 1950. Part I reprinted from August, 1950, PROCEEDINGS; Part II reprinted from September, 1950, PROCEEDINGS.....	\$1.25
52 IRE 7.S2 Standards on Gas-Filled Radiation Counter Tubes: Methods of Testing, 1952. Adopted by ASA. (ASA C60.11-1954). Reprinted from the August, 1952, PROCEEDINGS.....	\$0.75
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56 IRE 7.S2 Standards on Electron Devices: Definitions of Terms Related to Storage Tubes, 1956. Reprinted from the April, 1956, PROCEEDINGS.....	\$0.25
57 IRE 7.S2 Standards on Electron Tubes: Definitions of Terms, 1957. Reprinted from the July, 1957, PROCEEDINGS.....	\$1.00

(Continued on page 16A)

Calendar of Coming Events and Authors' Deadlines*

(Continued from page 14A).

- Prod. Tech. Symp., Villa Hotel, San Mateo, Calif., June 4-5
- Int'l Conf. on Info. Processing, UNESCO House, Paris, France, June 15-20
- Int'l Symp. on Circuit & Information Theory, Univ. of Calif. at Los Angeles, Los Angeles, Calif., June 16-18 (DL*: Dec. 22, Dr. G. L. Turin, Hughes Research Labs., Culver City, Calif.)
- Nat'l Conv. on Mil. Elec., Sheraton Park Hotel, Washington, D. C., June 29-July 1
- WESCON, San Francisco, Calif., Aug. 18-21
- Nat'l Symp. on Telemetry, Civic Aud. & Whitcomb Hotel, San Francisco, Calif., Sept. 28-30
- IRE Canadian Conv., Toronto, Can., Oct. 7-9
- Nat'l Elec. Conf., Sherman Hotel, Chicago, Ill., Oct. 12-15
- East Coast Conf. on Aero. and Nav. Elec., Baltimore, Md., Oct. 26-28
- Electron Devices Mtg., Shoreham Hotel, Washington, D. C., Oct. 29-31
- Nat'l Conf. on Automatic Control, New Sheraton Hotel, Dallas, Tex., Nov. 4-6
- Radio Fall Mtg., Syracuse, N. Y., Nov. 9-11
- Eastern Joint Comp. Conf., Hotel Statler, Boston, Mass., Nov. 30-Dec. 3
- PGVC Annual Meeting, St. Petersburg, Fla., Dec.

1960

- Transistor and Solid-State Circuits Conf., Univ. of Pa., Phila., Pa., Feb. 11-12
- IRE National Conv., N. Y. Coliseum and Waldorf-Astoria Hotel, Mar. 21-24
- SWIRECO (Southwestern Regional Conference), Houston, Texas, Apr. 20-22
- Nat'l Aeronautical Electronics Conf., Dayton, Ohio, May 2-4
- Western Joint Computer Conf., San Francisco, Calif., May 2-6
- 7th Reg. Tech. Conf. & Trade Show, Olympic Hotel, Seattle, Wash., May 16-18
- Cong. Int'l Federation of Automatic Control, Moscow, USSR, June 25-July 9
- WESCON, Ambassador Hotel & Pan Pacific Aud., Los Angeles, Calif., Aug. 23-26
- Nat'l Symp. on Telemetry, Washington, D. C., Sept.
- Industrial Elec. Symp., Sept. 21-22
- Nat'l Elec. Conf., Chicago, Ill., Oct. 10-11
- East Coast Conf. on Aero. & Nav. Elec., Baltimore, Md., Oct. 24-26
- Electron Devices Mtg., Hotel Shoreham, Washington, D. C., Oct. 27-29
- Radio Fall Mtg., Hotel Syracuse, Syracuse, N. Y., Oct. 31, Nov. 1-2

* DL = Deadline for submitting abstracts.

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56 IRE 8.S1 Standards on Electronic Computers: Definitions of Terms, 1956.	
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51 IRE 9.S1 Standards on Facsimile: Temporary Test Standards, 1943.	\$0.20
56 IRE 9.S1 Standards on Facsimile: Definitions of Terms, 1956. Adopted by ASA. (ASA C16.30-1957).	
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55 IRE 10.S1 Standards on Industrial Electronics: Definitions of Industrial Electronics Terms, 1955.	
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53 IRE 11.S1 Standards on Modulation Systems: Definitions of Terms, 1953.	
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54 IRE 12.S1 Standards on Radio Aids to Navigation: Definitions of Terms, 1954. Adopted by ASA. (ASA C16.26-1955).	
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49 IRE 14.S1 Standards on Piezoelectric Crystals, 1949. Adopted by ASA. (ASA C83.3-1951, R 1954).	
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57 IRE 14.S1 Standards on Piezoelectric Crystals—The Piezoelectric Vibrator: Definitions and Methods of Measurement, 1957.	
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5E IRE 14.S1 Standards on Piezoelectric Crystals: Determination of the Elastic, Piezoelectric, and Dielectric Constants—The Electromechanical Coupling Factor, 1958.	
Reprinted from the April, 1958, PROCEEDINGS.....	\$0.75
55 IRE 15.S1 Standards on Pulses: Methods of Measurements of Pulse Quantities, 1955. Adopted by ASA. (ASA C16.28-1956).	
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49 IRE 16.S1 Standards on Railroad and Vehicular Communications: Methods of Testing, 1949.	
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(Continued on page 18A)



Professor H. Ollendorff of the Technion, Israel Institute of Technology, delivers his paper at the opening session of the third National Convention of Electronic Engineers in Israel.

ISRAEL SECTION COSPONSORS THIRD NATIONAL CONVENTION OF ELECTRONIC ENGINEERS

For the third consecutive year, the Israel Section of the IRE was a cosponsor of the National Convention of Electronic Engineers. The Technion, Israel Institute of Technology, was host to this year's convention, which was held June 16-17 on the Technion campus on Mt. Carmel, Haifa.

The convention consisted of five sessions and a round-table discussion. In addition, a guided tour through the electronic laboratories of the School of Electrical Engineering and the Einstein Institute of Physics was organized for the benefit of those attending the convention.

The opening session was attended by 450 electronic engineers, representing research and development, industry, government and the armed forces, and trade and tutoring.

STRATO-LAB SYMPOSIUM INVITES PAPERS

The aim of the current Office of Naval Research Strato-Lab program is to make available to academic, industrial, and government scientists a manned, sealed, balloon-borne laboratory 20 to 25 miles above the earth, for purposes of research, environmental testing, and systems experimentation.

If this new research tool being offered to scientists for their explorations is to have maximum usefulness, each prospective user must have the opportunity to participate in determining its specifications. How a research objective is to be achieved, what particular instrumentation will be employed, what assumptions are made concerning the platform, will have to be determined for each experiment so that the functional requirements imposed on the basic Strato-Lab vehicle will become more or less evident.

Accordingly, ONR has asked Vitro Laboratories to put these questions before the scientific community: Would a manned balloon-borne stratospheric laboratory assist or further your research and development activities? How? What functional requirements, i.e., stability, weight, etc., would these activities impose on the Strato-Lab?

In order to provide a forum for discussion, Vitro Laboratories, ONR, and the Institute of Aeronautical Sciences plan to hold a joint symposium at the end of January, 1959, dealing with Strato-Lab applications. Papers describing possible such applications are invited. For further details, contact J. J. Freeman, Vitro Laboratories, 14000 Georgia Ave., Silver Spring, Md.

How Radar Got Its Name

Before Columbus, radar had no name. It was called "the thing with no name."

Aboard the Santa Maria, however, "the thing with no name" behaved in a most startling manner. No matter which way the antenna was pointed, the scope, like a rear view mirror, showed only where the ship had been — not where it was going. This phenomenon was most unnerving to all hands, since it necessitated the ship's going backwards much of the time . . . a condition

that gave rise, among other things, to a peculiar kind of mariner's nausea that came to be known as "throwing down".

So it is hardly surprising that on the morning of October 12, 1492, Columbus found himself on the rocks at San Salvador. Once on land, the crew re-christened the thing with no name and called it "radar" — the thing that looks the same way coming or going.

A few days later, the radar operator discovered the trouble: the tubes had been inserted upside down. Columbus was so grateful he bestowed upon him the Order of Camob . . . which, of course is Bomac spelled backwards.

No. 11 of a series . . . BOMAC LOOKS AT RADAR THROUGH THE AGES



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56 IRE 28.S2 Standards on Solid-State Devices: Methods of Testing Transistors, 1956. Reprinted from the November, 1956, PROCEEDINGS.....	\$0.80

AIR FORCE MARS ANNOUNCES BROADCASTING SCHEDULE

The Air Force MARS Eastern Technical Network, which broadcasts every Sunday from 2-4 P.M. (EST) on 3295, 7540, and 15,715 kc, announces the following programs:

December 7—"Navigation by Electronics," E. N. Storrs, Chief, Navigation Lab, Directorate of Control and Guidance, Rome Air Development Center.

December 14—"New Concepts in Communication Systems," A. A. Kunze, Directorate of Communications, RADC.

December 21—"Uni-Directional Antennas," A. J. Beauchamp and M. A. Diab, Directorate of Control and Guidance, RADC.

December 28—"Impact of Solid State Physics in Electronics," J. J. Naresky, Chief, Applied Physics Branch, Directorate of Technical Services, RADC.

January 4—Vacation Day.

ARMY MARS LISTS SCHEDULE

The Army MARS technical network, operating at 4030-kc upper sideband on Wednesday evenings at 9 P.M., will broadcast the following programs:

December 3—"International Radio Communication Systems," E. D. Becken, Assistant Vice-President and Chief Operations Engineer, RCA Communications Co.

December 10—"FM Multiplex Stereo System," M. G. Crosby, President, Crosby Labs.

December 17—"VHF Radio Propagation," E. P. Tilton, VHF Editor, American Radio Relay League.

December 24 and 31—Holidays.

OBITUARY

Donald K. Lippincott (M'28-SM'43), a partner of Lippincott, Smith and Ralls, patent attorneys of San Francisco, Calif., died recently. He was the first vice-chairman of the San Francisco Section of the IRE and later became the Section's chairman.

He was born in Huntsville, Ala., on December 3, 1889, and received the B.S.E.E. degree from the University of California at Berkeley in 1913. His legal education was obtained at San Francisco Law School, Hastings College of Law, Hastings, Neb., and George Washington University, Washington, D. C.

Until 1927 his activities were mainly in

the engineering field. He designed one of the earliest of the single-dial-control tuned radio frequency receivers marketed commercially on a national scale.

In June, 1927, he first entered patent practice, as an associate of Charles S. Evans in San Francisco, and handled cases dealing principally with radio and electrical and acoustic arts. In 1930 he entered private practice, and three years later formed the patent firm of Lippincott and Metcalf, where he acted as consulting engineer as well as patent attorney for clients in the radio, television, and electronics fields. On behalf of Philo T. Farnsworth he prosecuted original patents in television which were subsequently recognized by many groups.

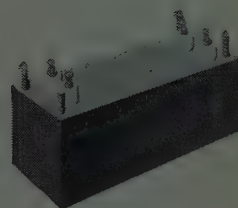
During World War II he entered active duty and was assigned first to the Radio Technical Commission for Aviation and Strategic Materials of the Research and Development Division, Office of the Chief Signal Officer; then to the National Defense Research Council (later the OSRD) and the National Inventors Council; then to the Legal Division of the Office of the Chief Signal Officer, later becoming the Division's director. As a representative of the Navy and the OSRD he held membership on the Army-Navy Patent Advisory Board, the Government Radar Patent Program Committee, and many other committees.

His services to the government during the war saved hundreds of millions of dollars. The Signal Corps patent licensing program, which he proposed, was the first systematic program within the Armed Services for obtaining licenses under patents used by them, instead of requiring the patentee to sue the government in the Court of Claims. The details of the program were formulated and administered by the Industry Committee, of which he was chairman. For this work he was cited and awarded the Legion of Merit.

In association with Carol Wilson he negotiated the "Company A-Company B" agreements relating to the interchange of radar information between British and American producers of radio and radar equipment. He also established the London, England, Signal Patent Agency, through which licenses to the U. S. or British Government under patents owned in the other country were negotiated.

Following the war's termination he acted as special consultant on technical and patent matters for Automatic Electric Co. in Chicago, and returned to private patent practice in April, 1946. In 1949 he formed the firm of Lippincott and Smith, which became Lippincott, Smith and Ralls in 1957. Many of the applications for patents which he handled were in the microwave, color television, and television recording fields. One of his most recent activities was in connection with the Lawrence color-tube.

Mr. Lippincott was a member of the bar of the State of California and a registered professional engineer in that state. He was member and past president of the Patent Law Association of San Francisco and of the Engineers' Club of San Francisco. He was also a life member of the AIEE, a charter member of the Pacific Radio Trade Association, a member of the American Bar Association, the American Patent Law Association, the Bar Association of San Francisco, the California Historical Society, and the Union League Club of Chicago.



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Through advanced crystal filter production techniques and circuitry by Burnell & Co., it is now possible to overcome numerous design problems formerly believed insoluble with even the best individual toroidal components.

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Whether you need crystal filters of standard design or custom units engineered to specifications of center frequency, band width, selectivity and impedance level, the facilities of Burnell & Co. are at your disposal. Write for new Burnell Crystal Filter Bulletin XT-455.

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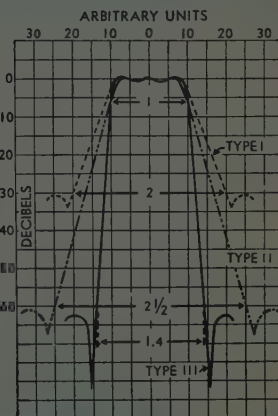
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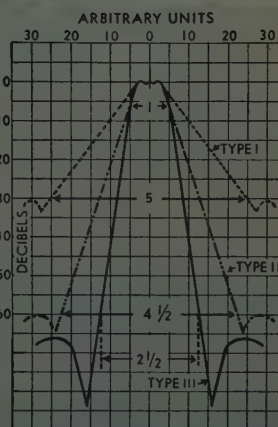
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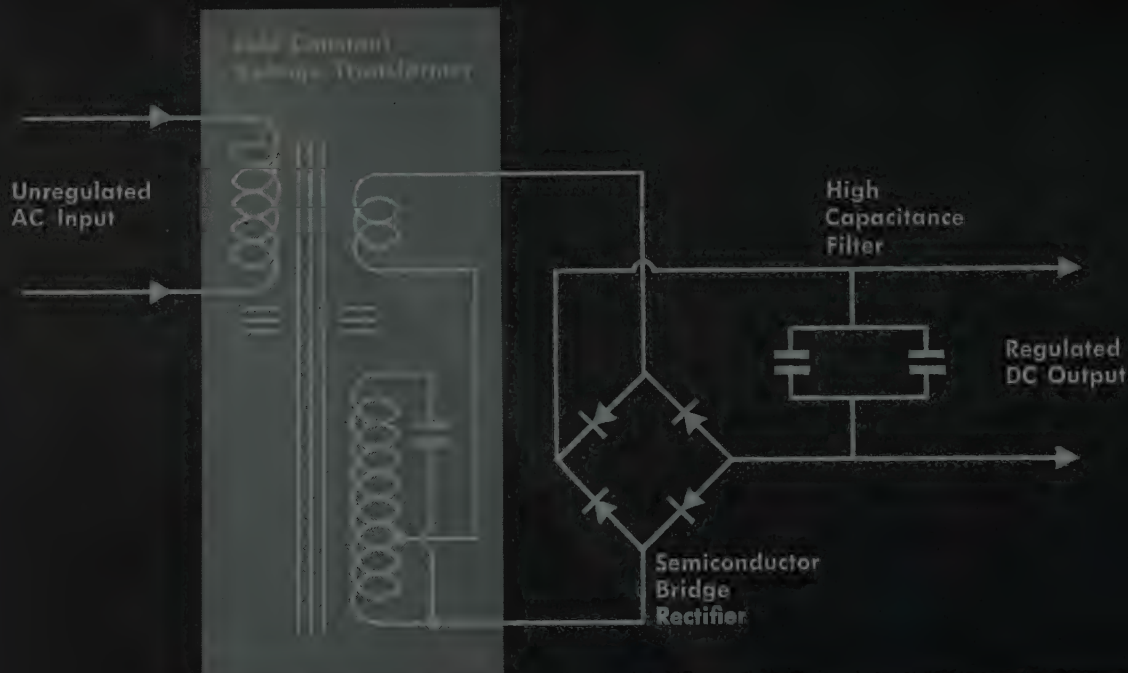
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Basic schematic diagram of Sola Constant Voltage DC Power Supply illustrates its design simplicity. Electrically and mechanically, these dc supplies are extremely reliable due to this basic simplicity.

SIMPLE, regulated DC power supply

Emerson said, "To be simple is to be great," and that perfectly describes the Sola Constant Voltage DC Power Supply. If you want to keep your apparatus as simple as you can (especially if it's basically complicated) this dc supply will do it.

You needn't worry about manual adjustments or maintenance in the field. There are no moving or expendable parts . . . no tubes. The entire supply is a unique combination of three components: 1) A special Sola Constant Voltage Transformer, 2) a

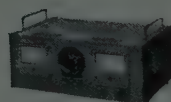
semiconductor rectifier, and 3) a high-capacitance filter. It's that simple. It's extremely dependable.

Regulation is $\pm 1\%$ against line voltage variations up to $\pm 10\%$. Ripple is within 1% rms. Outputs are in the "ampere range." It's particularly well-suited for use on apparatus with pulse, intermittent, or variable loads. Efficiency is high.

The Sola Constant Voltage DC Power Supply is simple, compact, very reliable, and moderately priced.



Fixed output — six ratings available from stock



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Custom-designed units produced to your specs

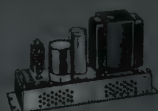
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For utmost accuracy, these new Precision Attenuators depend on mathematical law instead of resistivity

New "barrel" design (shown) on K and R band models; time-tested original design (same principle) on G through P band models. Phase shift constant with attenuation. High stability; unaffected by frequency, temperature or humidity changes. Direct reading; no charts or interpolation. Up to 15 watts capacity; simple, one-control tuning; large dial.



The new -hp- 382A series attenuators provide a completely reliable, true standard of attenuation for calibration or comparison measurements. Unlike waveguide-below-cutoff or resistive-film attenuators, no frequency correction is required. Attenuation is a function of mathematical laws of rotating electrical fields and is precisely accurate under all ambient conditions. Extremely compact, sturdy. For full details, call your -hp- representative or write direct.

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SPECIFICATIONS

	G382A	J382A	H382A	X382A	P382A	K382A	R382A
Frequency Range, KMC:	3.95 - 5.85	5.3 - 8.2	7.0 - 10.0	8.2 - 12.4	12.4 - 18.0	18.0 - 26.5	26.5 - 40.0
Waveguide Size:	2 x 1"	1½ x ¾"	1¼ x ⅝"	1 x 1.2"	0.702 x 0.391"	½ x ¼"	0.36 x 0.22"
Power-handling capacity, watts:*	15	10	10	10	5	3	2
Price:	\$500.00	\$350.00	\$350.00	\$250.00	\$275.00	\$425.00	\$450.00

*Average, continuous duty.

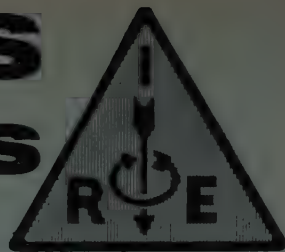
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standard of measuring speed and accuracy



NEWS New Products



Strain Indicator

A new portable, direct reading strain indicator, the Model DR-10, which provides continuous indication of static and dynamic strain with a minimum of operator adjustment is announced by Bytrex Corp., 294 Centre St., Newton 58, Mass. Strain is indicated directly on a wide scale meter eliminating the necessity to balance the instrument.



Wide range coarse and fine zero adjustments permit setting the instrument to zero for all initial unbalance conditions. The instrument requires no warmup, operates with two or four arm bridges, covers a range of 60,000 microinches per inch, is equipped with an oscilloscope jack and gage factor control and is suitable for operation with gage resistances of 60 to 1000 ohms.

Designed for use with all commercially available strain gages and strain gage transducers, the unit operates from four self-contained standard flashlight batteries with a guaranteed minimum life of 100 hours.

A unique feature of the DR-10 is that it indicates a true average of oscillating strain down to a few cps.

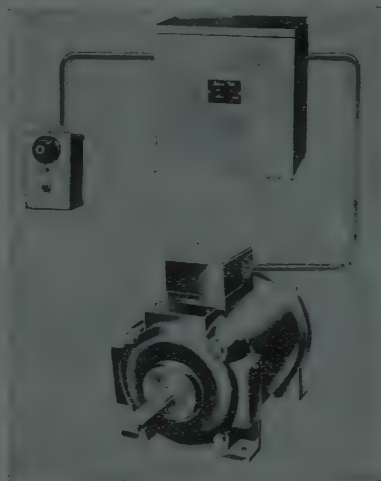
Contained in a hardwood case 11×8½×6 inches, the unit weighs less than 7 pounds.

Adjustable Speed Drives

Servo-Tek Products Co., Inc., 1086 Goffle Rd., Hawthorne, N. J., has announced a complete new line of adjustable-

These manufacturers have invited PROCEEDINGS readers to write for literature and further technical information. Please mention your IRE affiliation.

speed drives known as the precision series. These adjustable-speed drives incorporate totally enclosed fan-cooled motors for better protection from environmental conditions.



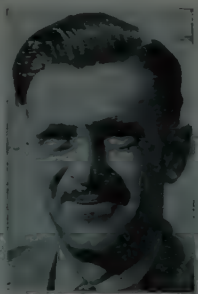
The new line is available in various horsepower, up to and including ¾ hp, and features regulation in the order of ½ of 1 per cent throughout a speed range as high as 100:1. All models can be continuously operated at full torque even at the lowest speeds.

In addition to the precision series, other model drives are available with less exacting specifications. For complete information write to Servo-Tek.

CG Electronics Name Tillman

Appointment of John E. Tillman as plant manager of CG Electronics Corp., a division of Gulton Industries, Inc., Albuquerque, N. M., has been announced by Harold Paulsen, general manager.

According to Paulsen, Tillman will supervise the production and internal operation of the company's antenna, telemetry, digital and special products departments. The company is a producer of radio control equipment.



Tillman attended Bridgeport Engineering Institute and the University of New Mexico, specializing in advanced communications engineering and management courses. He has had six patents issued as a result of his work.

Prior to joining Gulton Industries, Tillman performed production and engineering assignments in radio communications for the General Electric Co., for more than 10 years. In addition, he was a project engineer for Dalmo-Victor Co., chief engineer for Aviola Radio Corp., and department manager for the Sandia Corp.

Ferrite Switch

A low-power X-band ferrite switch for on-off applications has just been introduced by Raytheon Manufacturing Co., Special Microwave Device Group, Waltham 54, Mass.

The unit, Model SXL1, provides a minimum isolation of 25 db with an insertion loss of 0.5 db (maximum). Multiples of this isolation can be obtained by connecting several SXL1's in series.

Weight is 15 ounces; over-all length, 1.7 inches.



The company, which has already introduced numerous microwave ferrite devices including isolators and circulators, has other types of ferrite switches under development.

Data sheets are available from the firm.

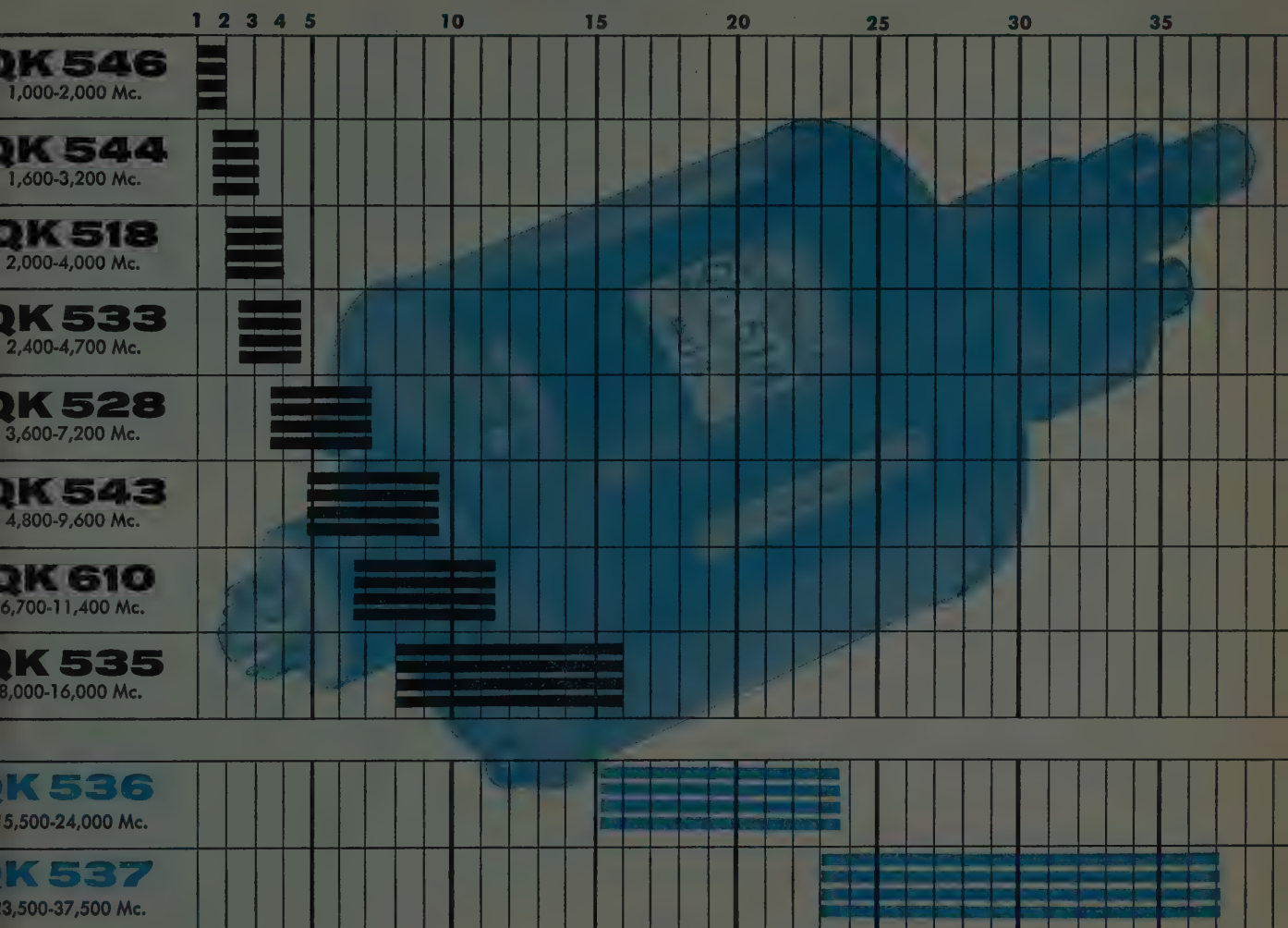
ORRadio Names Petrig Chief Engineer

ORRadio Industries, Inc., Shamrock Circle, Opelika, Ala., has named David Petrig Chief Engineer of the Manufacturing Division, company officials have an-

(Continued on page 25A)

VOLTAGE TUNABLE

In Thousands—Mc.



NOW — 2 New Raytheon Backward Wave Oscillators DOUBLE FREQUENCY COVERAGE



Specifications—QK 518. Frequency: 2,000-4,000 Mc. Rapid electronic tuning by varying delay line voltage from 150-1,500 v. Power output: 0.1 to 1 w. Complete with compact permanent magnet. Approximate maximum dimensions: 10" long, 4 3/8" high, 4 7/8" wide.

The most complete line in the industry now tunes from 1,000 to 37,500 Mc.

Wide, rapid electronic tuning—1,000 Mc. to 37,500 Mc.—is one outstanding performance advantage in Raytheon's extending line of Backward Wave Oscillators. Others are: permanent magnet focusing; high signal-to-noise ratio; operation under conditions of amplitude or pulse modulation.

Raytheon Backward Wave Oscillators are gaining wide acceptance in micro-

wave equipment applications as local oscillators for radar receivers and as signal generators.

Our development laboratories can tailor tubes for specific requirements including narrower band, lower voltage, or higher power for primary transmitter use. Any question you may have will be answered promptly, without cost or obligation.

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Raytheon makes: Magnetrons and Klystrons, Backward Wave Oscillators, Traveling Wave Tubes, Storage Tubes, Power Tubes, Miniature and Sub-Miniature Tubes, Semiconductor Products, Ceramics and Ceramic Assemblies.



Excellence in Electronics

FIRST LONG DISTANCE TROPO SCATTER SYSTEM PROVES

- SSB best for long tropo hops
- Longer high-quality hops now feasible
- High power is no problem with G-E amplifier

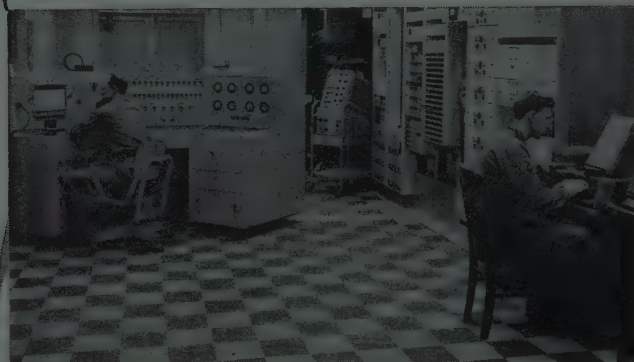


Operation of the world's first long distance single sideband tropospheric scatter system proves the practicality of SSB for over-the-horizon hops of several hundred miles. Spanning 640 miles between sites near Boston and Winston-Salem, multi-channel voice and teletype communications are maintained with high reliability.

With this system General Electric demonstrates the inherent advantages of SSB for long distance transmission: the ability to get more wide-band signal over long one-hop distances with less power, at less cost.



Klystron power amplifier of new design, featuring higher efficiency, reliability and lower operating cost. The entire system was designed by MIT Lincoln Laboratory in conjunction with Air Force Air Research and Development Command.



Control room showing control console and teletype machines. The system has been designed for ease of maintenance and operation to cope with extreme weather conditions.

When considering long-distance communications, remember General Electric's many years of experience in the design and manufacture of high power amplifiers, a key limiting factor in tropo scatter system design. And G-E engineers possess the practical system "know-how" so essential in the design and installation of long-range communication systems. Call these engineers to study your requirements. Military-Industrial Sales Technical Products Department, General Electric Company, Electronics Park, Syracuse, New York.

Progress Is Our Most Important Product

GENERAL  ELECTRIC



NEWS New Products



These manufacturers have invited PROCEEDINGS readers to write for literature and further technical information. Please mention your IRE affiliation.
(Continued from page 22A)

nounced. Petrig was formerly in the engineering section of the manufacturing division.

Petrig came to ORRadio with an extensive background and considerable experience in machine design and project engineering. In his new position he will be concerned with manufacturing methods and process development and adaptation of equipment, not only for present production but also for future plant expansion.

A native of Seattle, Washington, Petrig attended the University of Washington and graduated (1947) from the University of California with a B.S. in Mechanical Engineering. During World War II he served five years with Army Ordnance Procurement.



$\frac{1}{4}$ Inch Trimmer Potentiometers

Designed for horizontal-mounting applications by Miniature Electronic Components Corp., Holbrook, Mass., these trimmer potentiometers which measure $\frac{1}{4}$ inch square by $\frac{3}{8}$ inches long are engineered and tested for operation under environmental extremes of heat, cold, humidity, vibration and shock encountered in airborne and missile applications.



Available for stud-mounting (Model MS-4) and leadmounting (Model MS-5) on printed wiring boards, both models feature low temperature-coefficient resistance wire, precious metal wiper, Mylar and Teflon insulation.

The units are rated at $\frac{1}{4}$ watt and are available in standard resistance values from 100 ohms to 10,000 ohms.

(Continued on page 26A)

LOOKING
FOR THE

SENSITIVE TYPE?



TRY
THIS
NUMBER **SV-1C/5000D**

The Advance type SV Sensitive Relay (shown at right) is $1\frac{1}{4}$ " high x $2\frac{1}{2}$ " long x $\frac{1}{4}$ " wide. Also available is the type SO Miniature Sensitive Type, $1\frac{1}{2}$ " high x $1\frac{1}{4}$ " long x $\frac{1}{4}$ " wide.



Advance type SV relays are ultra-sensitive, yet durable—dust-tight, yet fully adjustable. Contacts and all working parts are protected by a transparent molded plastic cover.

SPECIFICATIONS

Coil resistance: From .005 Ohms at .005 volts DC to 40,000 Ohms at 14.0 volts DC.

Nominal power required: Factory adjusted at .005 watts.

Contact rating: 1 amp resistive, .5 amps inductive at 115 volts AC or 26.5 volts DC.

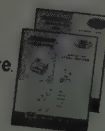
Contact arrangement: SPDT only.

Sensitivity can be adjusted from the 5-milliwatt factory setting by turning the vernier screws. Use the type SV in any DC circuit where power consumption is limited to a few thousandths of a watt.

Available from leading distributors

WRITE FOR COMPLETE DETAILS

Data sheets on the SV Sensitive Relay and the SO Miniature Sensitive Relay will be sent promptly.

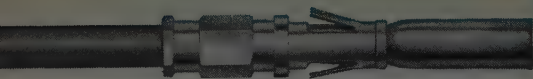


ADVANCE RELAYS

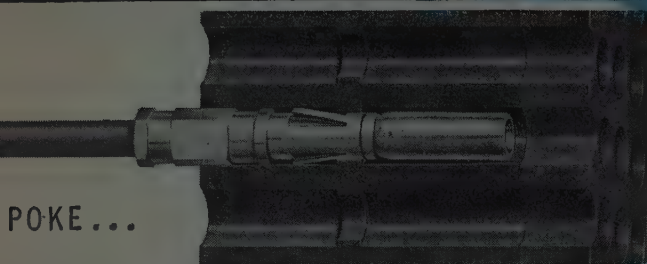
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A PRODUCT OF ELECTRONICS DIVISION
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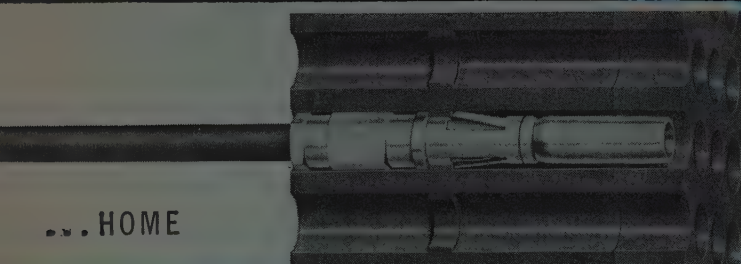
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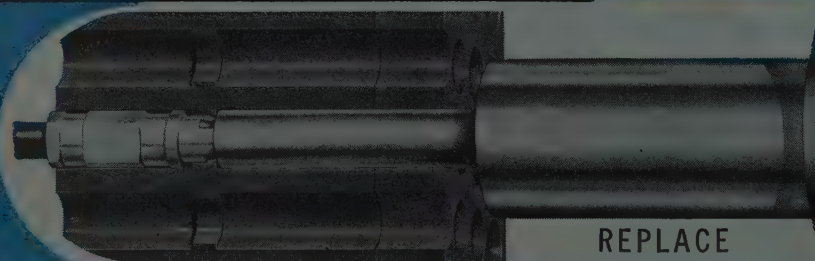
CRIMPED CONTACT



POKE...



...HOME



REPLACE

AMPHENOL POKE-HOME contacts*

AMPHENOL connectors with Poke Home contacts provide the electronics industry with a new and realistic answer to the problems of wire termination. Contacts, shipped separately from the connector, are crimped to their individual wire leads and then "poked home" into the insert. Each can be easily removed and replaced in case of circuit change.

Crimping of the contacts provides increased reliability through elimination of soldering. It permits inspection of each termination before insertion. And, mechanically and electrically, the millionth crimped termination is consistent with the first.

A Poke Home contact connector thus consists of individual circuits which may be strung through bulkheads or branched from different electrical sources and are quickly adaptable to any wiring change. Fewer manufacturing breaks in circuitry are assured; the number of steps in wire termination are reduced; the need for "J-boxes", terminal strips and other accessory components is similarly reduced.

*CONCEPT COVERED BY U.S. PATENT 2,419,018

Send for full information on AMPHENOL connectors with Poke Home contacts!

AMPHENOL ELECTRONICS CORPORATION
CHICAGO 50, ILLINOIS



NEWS New Products



These manufacturers have invited PROCEEDINGS readers to write for literature and further technical information. Please mention your IRE affiliation.

(Continued from page 25A)

New Firm Metallizes Ceramic Parts

William J. Callaghan, President of the Ceramic-Metal Assemblies Corp., on the left, and J. F. Murray, Jr., Engineering and Development, on the right, discuss firing and loading techniques of initial production samples of metallized ceramics. This is one of the first of many sample orders supplied by the new firm for customer testing.



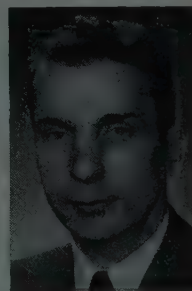
The new Latrobe, Pa., company has installed modern manufacturing equipment throughout its new plant for sealing, brazing, welding, soft soldering, gasketing and other processes required in the production of metallized ceramics, vacuum tight and high pressure ceramic to metal seals and other assemblies utilizing these components.

Geick Market Mgr. For Crosley Div.

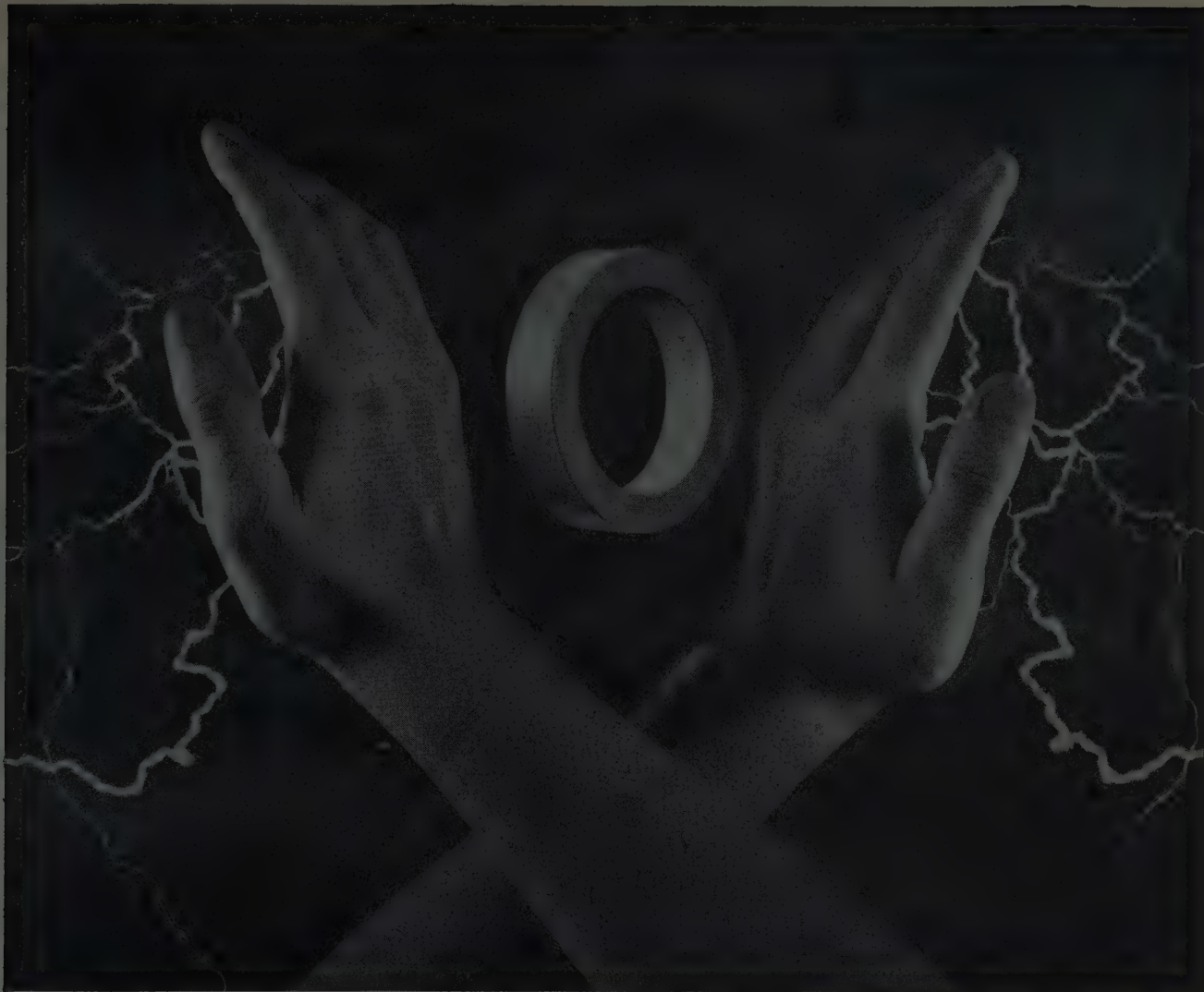
Appointment of George H. Geick to the post of Manager, Market Research and Planning in the Crosley Division of Avco Manufacturing Corp., Cincinnati, Ohio, was announced today by R. M. Bukaty, Vice President Marketing, Commercial Products.

Geick was formerly associated with the Mechanical Division of General Mills, Inc., as Manager of Engineering. He has graduate degrees in engineering from Purdue and Stanford and in 1950 received his M.B.A. from the Stanford Graduate School of Business. His earlier employment includes both engineering and marketing research work at Stanford Research Institute and general management experience at Emerson Radio and Phonograph Corp.

In his new position, Geick will be responsible for market research and product planning in the expanding commercial activity of the Avco-Crosley Div.



(Continued on page 88A)



GUARANTEED TO WITHSTAND 1,000 VOLTS!

GVB-finished tape wound core boxes drop your production costs

We have developed a radical new finish for aluminum boxes for tape wound cores. Your production department will glow with delight, for we guarantee this finish to withstand 1,000 volts (at 60 cycles) without taping!

GVB, for Guaranteed Voltage Breakdown (limits), is what we call this new finish. It is perfectly matched to our aluminum core boxes, for it will withstand temperatures from -70°F to 450°F . Potting techniques need not change, for GVB-finish lives happily with standard potting compounds.

By eliminating the need for taping the core box, you also eliminate a time consuming production step. By combining GVB-finish with our aluminum core box, we assure you a core capable of being vacuum impregnated down to 20 mm. of mercury.

And they are Performance-Guaranteed! Like all tape wound cores from Magnetics, Inc., aluminum-boxed or phenolic-boxed, you buy them with performance guaranteed to

published limits. The maximum and minimum limits are for B_m , B_r/B_m , H_1 and gain. This data is published for one, two, four and six mil Orthonol® and Hy Mu 80 tape cores.

GVB-finished cores are ready for you now. So are the published limits for all Magnetics, Inc. tape wound cores. Write today for more GVB details, and for your copy of the guaranteed performance limits: Dept. I-51, Magnetics, Inc., Butler, Pennsylvania.

MAGNETICS inc.

The Manufacturer's Responsibility to the User

YOUR REQUIREMENTS for increasingly higher performance in oscilloscopes inevitably lead to instruments of greater complexity, and therefore to an enlarged responsibility on the part of the instrument manufacturer to provide needed assistance in the field. As a user of Tektronix Instruments you have easy access to a large well-trained field organization, anxious to help with any problems that arise due to unfamiliarity with new circuits or other factors. All services described below are readily available through twenty-four Tektronix Field Offices in North America. Most of these services are also provided by more than twenty Tektronix Engineering Representatives in pertinent overseas locations.



Maintenance—Tektronix willingly assumes much of the responsibility for continued efficient operation of the instruments it manufactures. If you should experience a stubborn maintenance problem, your Field Engineer will gladly help you isolate the cause. Often a telephone discussion with him will help you get your instrument back into operation with minimum delay. If yours is a

large laboratory, your Field Engineer can be of service to your maintenance engineers by conducting informal classes on test and calibration procedures, trouble-shooting techniques, and general maintenance.

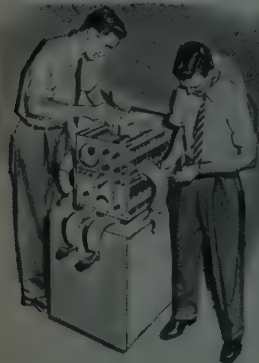
If you are responsible for the maintenance of a large quantity of Tektronix Instruments, ask your Field Engineer about the free factory training course in maintenance and calibration.

Operation—Your Tektronix Oscilloscope can be most useful to you when you are familiar with all control functions. Your Field Engineer will be glad to demonstrate the use of your instrument in various applications to help you become more familiar with its operation. If your instrument is to be used by several engineers, your Field Engineer will be happy to conduct informal classes on its operation in your laboratory.

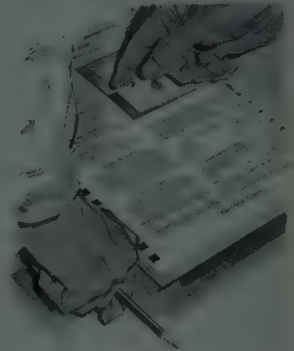


Instrument Reconditioning—An older Tektronix Oscilloscope, properly reconditioned, can give you many additional years of service. Your Field Engineer will gladly explain the advantages and limitations of factory reconditioning, and make the necessary arrangements if you decide in favor of it.

Many major repair and recalibration jobs can be performed at a nearby Field Repair Station. Ask your Field Engineer about this at-cost service to Tektronix customers.

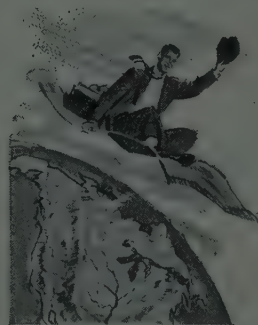


Applications—Perhaps the answers you need in a specific application can be obtained faster and easier through use of your Tektronix Oscilloscope. Your Field Engineer can help you find out, and if use of your oscilloscope is indicated, help you with procedures. He may also be able to suggest many time-saving uses for your oscilloscope in routine checks and measurements.



Ordering—There are many types of oscilloscopes, each designed for a specific application area. Your Field Engineer can help you select the one best suited to your present and future needs, and he will be happy to arrange a demonstration of the instrument... in your application if you so desire.

If you are a Purchasing Agent or Buyer, your Field Engineer or his secretary can help you with information on prices, terms, shipping estimates, and best method of transportation on instruments, accessories, and replacement parts.



Communications—Your Field Engineer is a valuable communication link between you and the factory. He knows the exact person to contact in each circumstance, and he can reach that person fast and easily. Let him help speed your communications with the factory on any problem related to your Tektronix Instruments.

Tektronix, Inc.

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Model LT 1095M (metered)	\$315
Model LT 2095	\$365
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Voltage Bands ...0-8, 8-16, 16-24, 24-32 VDC

Line Regulation ...Better than 0.15 per cent or 20 millivolts (whichever is greater). For input variations from 105-125 VAC.

Load Regulation... Better than 0.15 per cent or 20 millivolts (whichever is greater). For load variations from 0 to full load.

AC Input 105-125 VAC, 50-400 CPS

Electrical Over-

load Protection ...Magnetic circuit breaker, front panel mounted. Unit cannot be injured by short circuit or overload.

Thermal Over-

load Protection ...Thermostat, manual reset, rear of chassis. Thermal overload indicator light, front panel.

Size 3½" H x 19" W x 14⅜" D.

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for quicker and more
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CONDUCTANCE DESIGN OF ACTIVE CIRCUITS

*A New approach to the design
of active circuits!*

The non-linearity of electron tubes and transistors has for many years greatly complicated the design of active circuits associated with these devices. This book presents a proven method of overcoming these complications.

The conductance approach utilizes a technique whereby a non-linear circuit may be linearized on a point-by-point basis. This definitive book explains and illustrates the theory and mathematics involved in this technique.

It presents the conductance technique as applied to the design of a wide variety of vacuum tube and transistor amplifier, mixer, and oscillator circuitry in the broadest sense. To make the mathematics completely understandable, practical numerical examples are given throughout.

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This manual, a companion volume to Conductance Design of Active Circuits, is the designer's tool complete with tube curves, tables, and explanations for applying the conductance approach to electronic circuit design problems. It will enable designers, engineers, engineering students, and laboratory technicians to select the proper tubes and their associated components to apply the conductance approach. It has been shown that the non-linear circuit may be linearized on a point-by-point basis if adequate data on the small-signal characteristics of the non-linear devices are available. Based on this knowledge, the author has constructed new curves to enable design using small-signal parameters to predict large-signal circuit performance.

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IRE People



Dr. Raymond K. Masnaghetti (S'52-A'53) has been promoted to manager of the research and analysis department in the Development Division at Stavid Engineering, Inc., Plainfield, New Jersey.

He received the Ph.D. degree in electrical engineering from Purdue University and served there as an assistant professor until joining Stavid earlier this year as an engineering consultant. He has done work in transistor circuitry research, mathematical problems applied to radar design, and studies on military communications systems. He is presently engaged in operations research applied to radar systems development.

Dr. Masnaghetti is a member of the American Society for Engineering Education and several honorary engineering societies.



R. MASNAGHETTI

The National Science Foundation announced today the appointment of Arthur H. Waynick (A'43-SM'46-F'57) as program director for engineering sciences, Division of Mathematical, Physical, and Engineering Sciences. Dr. Waynick is on leave from Pennsylvania State University, where since 1948 he has been professor and chairman of the electrical engineering department and director of the Ionosphere Research Laboratory.

He received the B.S. and M.S. degrees from Wayne University in Detroit, where from 1935 to 1937 he was an instructor of physics. He obtained the D.Sc. degree in communications engineering from Harvard University in 1943 after previous study at Cambridge from 1937 to 1939. In 1939 he returned to Wayne University as assistant professor of physics.

From 1940 to 1945, he was associated with the Harvard University Underwater Sound Laboratory as head of the electronics section. In 1945 he moved to Pennsylvania State University with the Laboratory, which became known as the Ordnance Research Laboratory, and has been there ever since.

Dr. Waynick is a member of the Institute of Electrical Engineers, the American Geophysical Union, the American Society of Engineering Education, Eta Kappa Nu, Sigma Pi Sigma, Sigma Xi, and the USA National Committee of the International Scientific Radio Union. He presently serves on the Foundation's Advisory Committee on Radio Astronomy, the National Bureau of Standards' Advisory Committee on Radio, and the International Geophysical Year's Technical Panel on Ionospheric

Physics, as well as their Working Group on Satellite Ionospheric Measurements. He has received the Navy Ordnance Development Award (1945), the Office of Scientific Research and Development Award (1945) the American Institute of Electrical Engineering's Electronics Award (1950-51), a Guggenheim Fellowship (1954-55), and the Distinguished Alumni Award of Wayne State University (1957). He has written numerous technical articles.

A. S. Saphier, President of General Bronze Corporation, has announced the promotion of Ira Kamen (M'48-SM'52) to Vice-president. Mr. Kamen is currently vice-president of GB Electronics Corporation, a wholly-owned subsidiary of General Bronze.

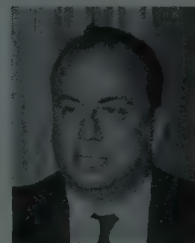
He will direct the sales and research programs for GB Electronics in Valley Stream, Long Island, one of the world's largest design, development, and production facilities devoted exclusively to missile ground support equipment and integrated antenna systems for communications, radio telescope, satellite and missile tracking applications.

Mr. Kamen's affiliation with General Bronze has continued for more than eight years. He is a well-known electronics engineer and the author of five important technical texts, as well as more than 150 trade and technical articles. Among the many patents he holds is an antenna coupling system assigned to the Radio Corporation of America, which forms the distribution network for all the RCA "Antennaplex" systems.

Federal Pacific Electric Company has announced two new engineering appointments, those of Dr. Andrew A. Halacsy as a staff development specialist and Gordon O. Perkins (S'47-A'49-M'55) as manager of the company's development engineering department, Eastern Switchgear Division.

Mr. Perkins was previously employed for ten years by the I-T-E Circuit Breaker Company, Philadelphia.

(Continued on page 34A)



I. KAMEN



G. O. PERKINS

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**ruggedized...miniaturized
peak performance...**

Kuthe KU-73

CERAMIC HIGH POWER THYRATRON



Characteristics of KU-73 Ceramic Thyatron

epx.	25.0 kv.
ib	1000 amp.
Ip (RMS)	40 amp.
Pb (epy x prr x ib) . . .	20 x 10 ⁹
Height.	5.75 in.
Diameter.	3.50 in.

HERE is a brand new hydrogen thyatron in ceramic envelope—for most severe environmental requirements in switch and network discharge applications.

The KU-73 shown here is a 25 kv/1000 amp. peak thyatron, comparable in ratings to glass type 5948/1754, more than three times its size. It is only 5¾" high and 3½" in diameter . . . while its glass counterpart is 15¾" high by 5⅛". Because it is ceramic, the KU-73 has far greater ability to stand shock and vibration. It can operate at ambient temperatures up to 125°C. Ratings can be substantially increased by air or oil cooling . . . readily accomplished because of the efficient dissipation possible with this compact, thermally efficient design.

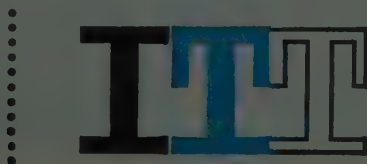
The KU-73 incorporates an internal low temperature hydrogen reservoir for long life and highly stable performance characteristics. Jitter is less than 1 millimicrosecond.

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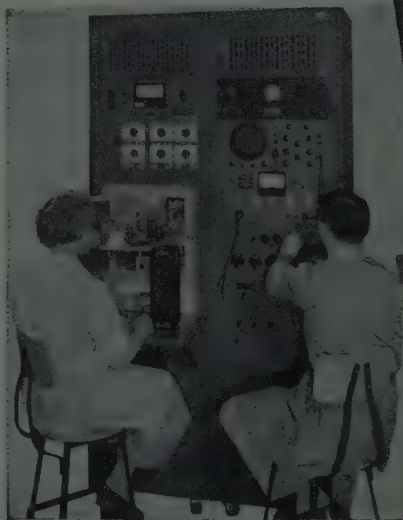
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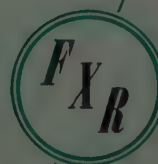
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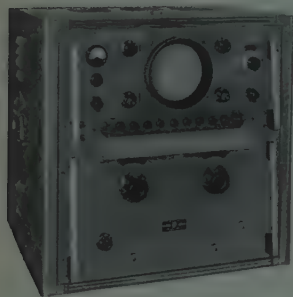
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New printed circuit Standing Wave Amplifier.

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Type L701A: 950 to 2000 Mc/s (Fund.)
Type S701A: 1900 to 4000 Mc/s (Fund.)

Harmonic Operation: to 16,000 Mc/s
Swept IF: 7 Kc and 50 Kc
Sweep Width: 50 Mc
RF Attenuator: 100 db Range
Video Markers



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Type L771B: 950 to 2000 Mc/s
Type S771B: 1900 to 4000 Mc/s
Type C772A: 3950 to 8200 Mc/s
Type X772A: 7000 to 11,000 Mc/s
Output Power: 50 mw (average)
Direct Reading Frequency Dial: 1%
Internal Modulation: Pulsed, Square Wave, C.W.
Integral RF Level Set Attenuator



UNIVERSAL RATIONOMETER, 811

(COMBINED RATIO METER AND
STANDING WAVE AMPLIFIER)

RATIO METER—1000 cps operation
VSWR Ranges: 1.02 to 1.22, 1.20 to ∞
Reflection Coefficient: .01 to .1, .1 to 1.0
Other Scales: db, Slotted Line VSWR
Standing Wave Amplifier—1000 cps operation
Range: 70 db in 10 db steps
Noise Level: .03 mv
Scales: VSWR, db, Expanded VSWR
Bolometer Bias: 4.5 and 8.75 ma
Input Impedance: 200 ohms or 200 K ohms



UNIVERSAL KLYSTRON POWER SUPPLY, 815

Beam: 200 to 2000 V, 125 ma max.,
1800 to 3600 V, 100 ma or 250
W max.
Reflector: 0 to 1000 V
Control Grid: -300 to 0 to +150 V,
5 ma max.
Regulation: 0.03%
Ripple: 3 mv max.
Internal Reflector Modulation:
Square Wave, Pulse, Sawtooth,
Sine Wave



UNIVERSAL MICROWAVE POWER SUPPLY, 817

Helix or Beam: 0 to 1800 V, 125 ma max.
1700 to 3500 V, 100 ma or 250 W max.
Collector: 0 to 300 V, 100 ma max.
Anode: 0 to 600 V, 60 ma max.
G-1: 0 to 300 V, 5 ma max.
G-2 or Reflector: 0 to ± 1200 , 1 ma max.
G-3: 0 to ± 750 , 1 ma max.
G-4: 0 to ± 500 , 1 ma max.
Regulation: 0.03%. Ripple: 3 mv max.
Heater: 0 to 15 V D.C., Regulated.
Internal G-1 or G-2 Modulation: Sine Wave
Square Wave, Pulse, Sawtooth



KLYSTRON POWER SUPPLY, 819

Beam: 300 to 1000 V, 85 ma max.
Reflector: 0 to 900 V, 20 μ a max.
Control Grid: -300 to 0 to +150 V,
5 ma max.
Regulation: 1%
Ripple: 7 mv max.
Internal Reflector Modulation:
Square Wave, Pulse, Sawtooth

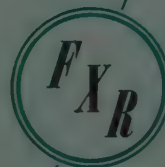


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**Rigid quality control extends average service
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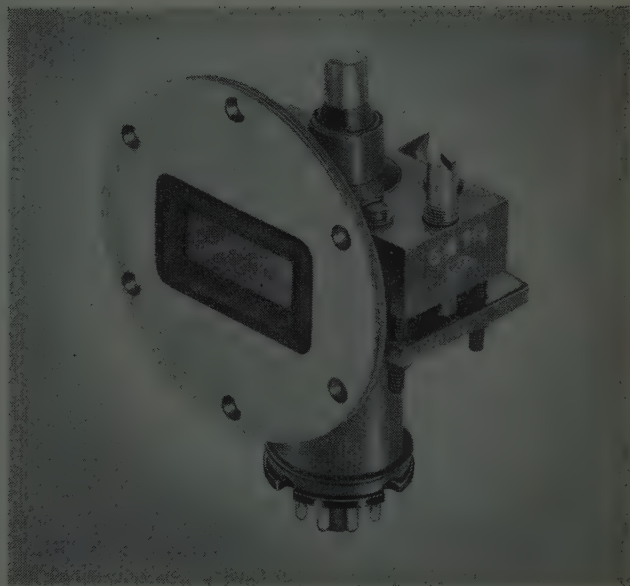
The Sylvania Klystron line covers over 20 different types from Disc Seal types to the C-Band metal types listed. Many other klystrons specially designed for specific equipments are also available. Contact your Sylvania representative or write direct for full information on the Sylvania Klystron line.

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Every Sylvania Klystron approved for shipment is *fully specified*. Beyond the information contained in ordinary data sheets, Sylvania offers full information on important characteristics such as:

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- Distortion
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Availability of complete and exact data on every important klystron characteristic helps cut the guesswork out of design for the microwave engineer. Equipment specifications can be met accurately, confidently, and design adjustments can be avoided. Get complete information when you order Klystrons—specify Sylvania.



Sylvania Microwave Relay Klystrons

Characteristics	TYPE		
	K-841B	K-840B	K-839B
Mechanical Tuning Range — MC	6125 — 6425	6575 — 6875	7125 — 7425
Resonator Voltage — Volts	750	750	750
Reflector Voltage — Volts	-250 to -400	-250 to -400	-250 to -400
Cathode Current — MA	80 (max)	80 (max)	80 (max)
Power Output — Watts	0.7 (min)	0.7 (min)	0.7 (min)
Heater Voltage — Volts	6.3	6.3	6.3
Heater Current — Amperes	0.8	0.8	0.8
Flange Mates with —	UG 343 A/U	UG 343 A/U	UG 343 A/U



SYLVANIA

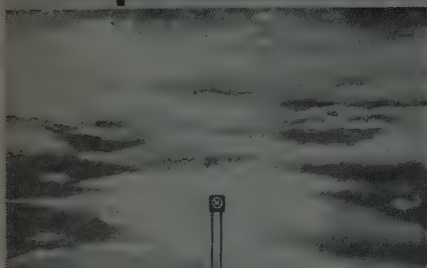
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IRE People



(Continued from page 30A)

Pa., where he supervised the company's 5-kv air circuit breaker development program. Before that, he was associated with General Electric Company in Philadelphia as a test engineer in the firm's local switch-gear plant.

A native of Collingdale, Penn., he received the B.E.E. degree from Clemson A & M College in Clemson, S. C., and the M.S.E.E. degree from the University of Pennsylvania's Moore School. A lieutenant in the U. S. Navy during World War II, he served as electrical officer at the demagnetizing station in Norfolk, Va., and as officer in charge of the Navy's de-gaussing range station, New York, N. Y.

Mr. Perkins is a member of the American Institute of Electrical Engineers, the National Society of Professional Engineers, and Franklin Institute. He holds several patents in the electrical field.



Dr. Allen V. Astin, director of the National Bureau of Standards, U. S. Department of Commerce, has announced the appointment of **Dr. Robert D. Huntoon** (A'40-SM '47-F'54) to the newly created position of deputy director. In this post, Dr. Huntoon will serve as alternate to the director in external matters and will exercise day-to-day direction and review of Bureau programs, working through the

associate directors for engineering, chemistry, the Boulder (Colo.) Laboratories, planning, and administration. He will continue to serve as associate director for physics.

He joined the Bureau staff in 1941, as one of the principal scientists concerned with the development of the radio proximity fuze, considered by many to be second in importance only to the atomic bomb among World War II scientific achievements. Since then he has been, at various times, chief of the electronics division, chief of the atomic and radiation physics division, acting chief of the central radio propagation laboratory, coordinator of Atomic Energy Commission projects at the Bureau, and director of the NBS Corona (Calif.) Laboratories, which are now operated by the Navy Bureau of Ordnance. In 1953, he was appointed associate director for physics.

In a wide and varied career, Dr. Huntoon has conducted or supervised research and engineering in numerous fields, including atomic beams, experimental nuclear physics, secondary emission phenomena, microwave measurements, electronic ordnance devices, atomic physics, guided missiles, digital computers, and fundamental physical constants. He is currently serving as chairman of a study group created by the House Appropriations Committee to investigate problems of reliability as they apply to weapons systems.

Born in Waterloo, Iowa, in 1909, he received the B.A. degree in physics from Iowa State Teachers College in 1932, and

(Continued on page 36A)

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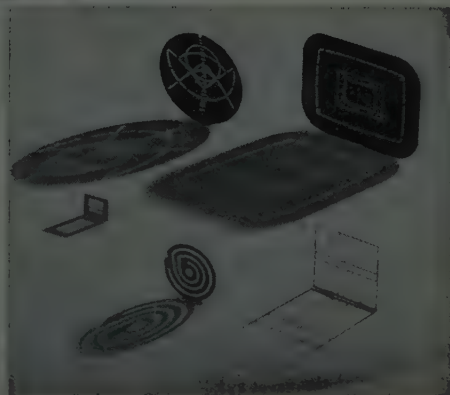
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IRE People



(Continued from page 34A)

the M.A. and Ph.D. degrees from the State University of Iowa in 1935 and 1938, respectively. Prior to coming to the Bureau he was an instructor of physics at New York University, and was a research physicist with the vacuum tube division of Sylva Electric Products, Inc.

Dr. Huntton has received a Presidential Certificate of Merit and a Department of Commerce Exceptional Service Award for V.T. tube contributions, a Washington Academy of Sciences Award in Physical Sciences, Certificates of Appreciation from the OSRD, War Department, and Secretary of War, a Naval Ordnance Development Award for contributions to electronic ordnance, and an Achievement Award from the Alumni of Iowa State Teachers College. He is a Fellow of the American Physical Society and a member of the Washington Academy of Sciences, the Philosophical Society of Washington, Sigma XI, and Kappa Delta Pi.



Edwin L. Davis (A'52-M'52-SM'56) has been appointed regional commercial engineer in Clifton, N. J., for the General Electric Receiving Tube Department. He will direct engineering liaison with manufacturers of industrial, entertainment, and military electronic equipment in circuit designs involving receiving tubes. Since 1955, he has been a commercial engineer handling internal sales of receiving tubes in Syracuse, N. Y.



E. L. DAVIS

After graduating from Alabama Polytechnic Institute, Auburn, Ala., with the B.S.E.E. degree in 1950, he joined the GE engineering test program, and took assignments in Pittsfield, Mass., Johnson City, N. Y., Owensboro, Ky., and Syracuse. He served as an application engineer and supervisor in application engineering in Owensboro from 1952 to 1955.

During World War II Mr. Davis served in the U. S. Navy as an electronic technician. He is treasurer of the Syracuse Toastmasters Club.



At the University of Michigan in Ann Arbor Stephen S. Attwood (SM'44) has been appointed dean of the College of Engineering and William G. Dow (M'39-SM'43-F'50) has been appointed chairman of the department of electrical engineering.

Dean Attwood has been associated with the University of Michigan as student and teacher since 1914. Born in Cleveland, Ohio, on May 29, 1897, he received the B.S. degree in mechanical engineering from the University in 1918 and the M.S. degree in electrical engineering in 1923. After

(Continued on page 38A)

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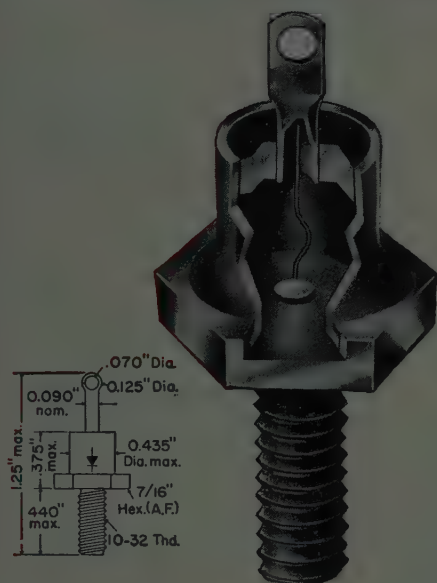
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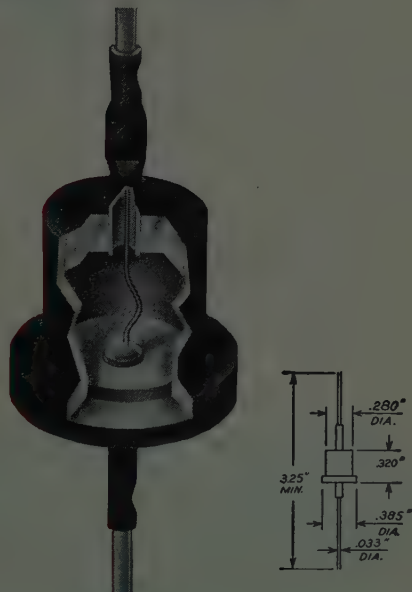
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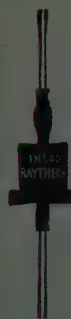
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TYPE	Peak Operating Voltage -65°C to +165°C	Ave. Rectified Current		Reverse Current (Max.) at Specified PIV, 25°C
	Volts	25°C Amps.	150°C Amps.	µA
1N253	95*	3.0	1.0*	10
1N254	190*	1.5	0.4*	10
1N255	380*	1.5	0.4*	10
1N256	570*	0.95	0.2*	20
CK846	100	3.5	1.0	2
CK847	200	3.5	1.0	2
CK848	300	3.5	1.0	2
CK849	400	3.5	1.0	2
CK850	500	3.5	1.0	2
CK851	600	3.5	1.0	2

1N253 through 1N256 available to MIL specifications.

*to +135°C



TYPE	Peak Operating Voltage -65°C to +165°C	Ave. Rectified Current		Reverse Current (Max.) at Specified PIV, 150°C
	Volts	25°C mA	150°C mA	mA
1N536	50	750	250	0.40
1N537	100	750	250	0.40
1N538	200	750	250	0.30
1N539	300	750	250	0.30
1N540	400	750	250	0.30
1N1095	500	750	250	0.30
1N547†	600	750	250	0.35

1N538, 1N540, 1N547 available to MIL specifications. †Same as 1N1095



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IRE People



(Continued from page 36A)

serving as an assistant engineering naval officer for a year, he became an instructor in electrical engineering in 1920. He subsequently was appointed assistant professor, associate professor, and, in 1937, professor. In 1953 he became chairman of the department of electrical engineering, and for the past year served as acting dean of the College of Engineering.

During World War II he was a member of the U. S. Propagation Mission to England and director of the Wave Propagation Group of the OSRD. Following the war he edited the three-volume "Summary Technical Report" of the NDRC Committee on Propagation.

Throughout his career on the university faculty he has been responsible for instruction and research in electromagnetic field theory. In 1953 he was chairman of the Faculty Committee for the University Centennial of Engineering. The committees of which he is currently a member are the Board of Governors of the Michigan Memorial-Phoenix Project for peaceful uses of atomic energy, the Executive Committee of the University of Michigan Research Institute, and the Willow Run Laboratories.

Dean Attwood is a Fellow of the AIEE and a member of the American Association for Engineering Education, the Engineering Society of Detroit, and the USA National Committee of URSI, and is a registered electrical engineer in the State of Michigan. He is the author of "Electric and Magnetic Fields," published by John Wiley and Sons in 1932, followed by revised editions in 1940 and 1949.

Professor Dow was born at Faribault, Minn., on September 30, 1895. He received the B.S. degree in electrical engineering in 1916 and the E.E. degree in 1917 from the University of Minnesota, and the M.S.E. degree from the University of Michigan in 1929.

For six years following World War I he was with the Westinghouse Electric and Manufacturing Company. Since 1926 he has been on the faculty of the University of Michigan, with two and a half years during World War II spent at the Radio Research Laboratory, Harvard University. There he was in charge of research and development on high-power microwave transmitters and tubes.

After returning to his duties as professor of electrical engineering at the University of Michigan, he was responsible for the initiation of major research activities in microwave electron tubes, particularly magnetrons and travelling-wave tubes, in upper atmosphere research using rocket vehicles, and in high-power gaseous electronics, and established the Electronic Defense Group, which has been active in varied fields of electronic circuitry, propagation, electron tube, and psychophysics studies. He also played an important part in establishing the Willow Run Laboratories of the University of Michigan, a very extensive and primarily electronic re-

(Continued on page 40A)

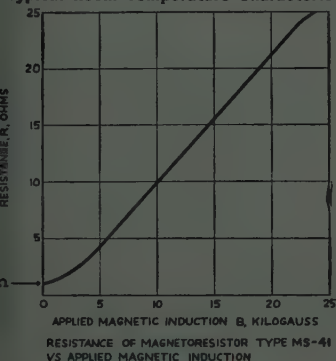
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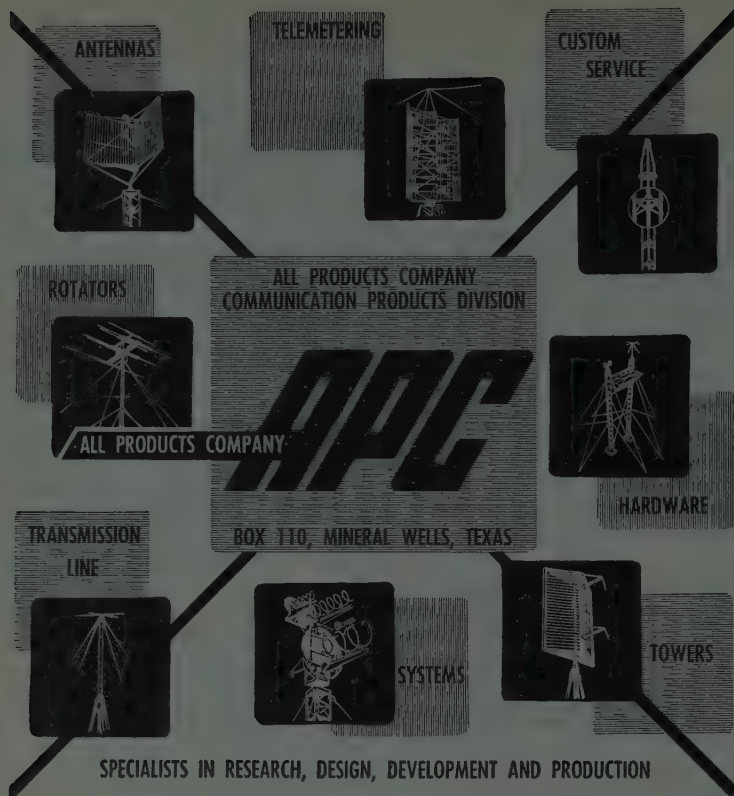
- ✓ contactless potentiometers
- ✓ amplifier
- ✓ voltage and current regulators
- ✓ control applications
- ✓ computer applications
- ✓ squaring devices
- ✓ modulators
- ✓ choppers
- ✓ transducers

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IRE People



(Continued from page 38A)

search activity which carries on important defense work integrated with the instructional program of the College of Engineering.

He is a member of the Scientific Advisory Committee of the Diamond Ordnance Fuze Laboratories, and a charter member of what is now called the Rocket and Satellite Research Panel. Since 1946 the Panel has been responsible for the planning and implementation of upper atmosphere rocket research carried on in the United States, and at its tenth anniversary it sponsored the first symposium on the use of satellites for space research.

Professor Dow originated the plan for operating high-level symposia for graduate credit in the form of four-week instructional courses on frontier electronic subjects, attracting nation-wide enrollment from universities, industries, and government laboratories. During World War II and in 1953 he made surveys of the vacuum tube research and development programs in European laboratories, and during the war he was a member of the Vacuum Tube Development Committee of the NDRC. He is the author of "Fundamentals of Engineering Electronics," published by John Wiley and Sons in 1937, revised edition in 1952, and co-author of "Very High Frequency Techniques," published by McGraw-Hill Book Co. in 1946.

At the University of Michigan he has served on various committees. He is a Fellow of the AIEE, a past chairman of the Board of Directors of the National Electronics Conference, and a registered electrical engineer in the State of Michigan.

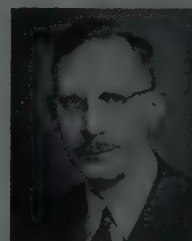


Hendrik W. Bode (M'41-SM'43-F'52), director of research in the physical sciences, and Jack A. Morton (A'36-SM'53-F'53), director of device development, have been elected vice-presidents of Bell Telephone Laboratories, effective October 1.

Dr. Bode, who has been associated with Bell Laboratories since 1926, will be in charge of one of two vice-presidential areas devoted to military development. He succeeds J. P. Molnar who was recently elected president of the Sandia Corporation and a vice-president of the Western Electric Company.

Mr. Morton will head a new vice-presidential area which is being established with the in-

(Continued on page 42A)



H. W. BODE



J. A. MORTON



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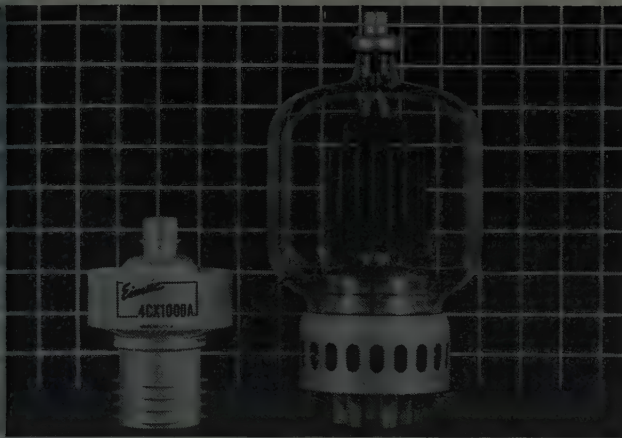
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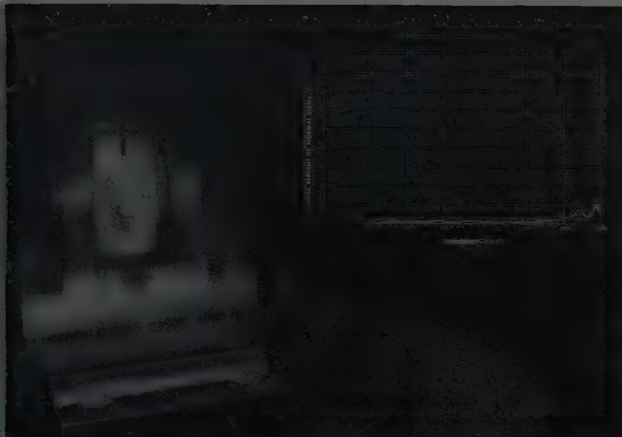
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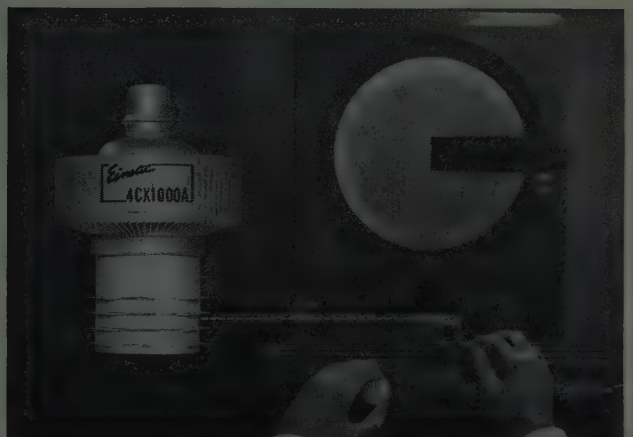
SMALLER SIZE



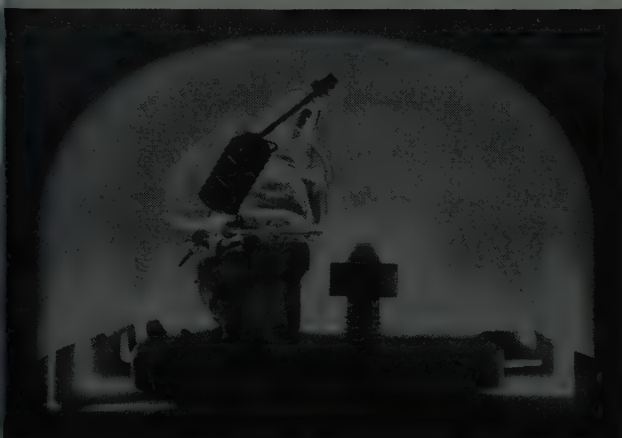
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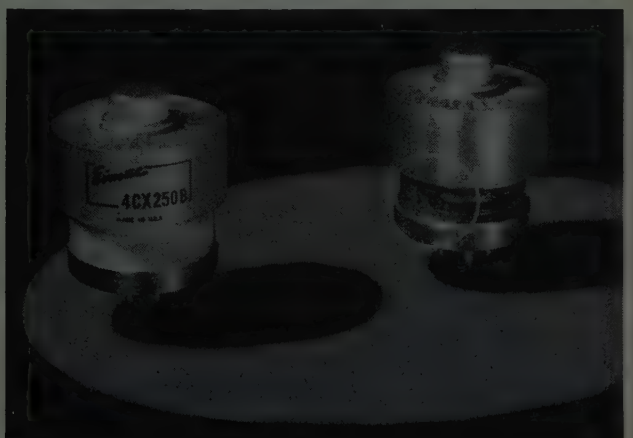
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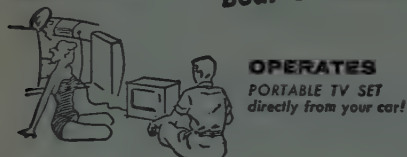
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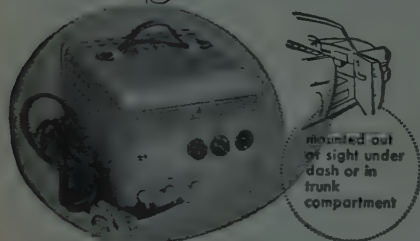
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IRE People



(Continued from page 40A)

creasing volume of work in device development, including transistors and other solid state devices, electron tubes, and electro-mechanical and passive devices. He joined the technical staff of Bell Laboratories in 1936.

Dr. Bode received the B.S. and M.S. degrees from Ohio State University in 1924 and 1926, respectively, and the Ph.D. degree from Columbia University in 1935.

During his first three years at the Laboratories, he was engaged in electric filter and equalizer design. He joined the mathematics research group in 1929, and specialized in research on electrical network theory and its application to long distance communication facilities. After the outbreak of World War II he turned to the development of electronic fire control devices, and in recognition of his contributions in this field was awarded the Presidential Certificate of Merit.

He was placed in charge of the mathematics research group in 1944, and in 1952 became director of mathematical research. He assumed the post of director of research in the physical sciences in October, 1955.

Especially since the war, he has made important contributions to the evolution of applied mathematics as an effective technique for application both in industry and in the broad field of modern military problems.

Dr. Bode is the author of a book on network theory and feedback amplifier design. He is a member of the National Academy of Sciences, a Fellow of the American Institute of Electrical Engineers and the American Physical Society, and a member of the American Mathematical Society and Phi Beta Kappa.

Mr. Morton received the B.S. degree in electrical engineering from Wayne University in 1935 and the M.S. degree in engineering from the University of Michigan in 1936.

During the early part of his Bell Laboratories career, he specialized in research on coaxial cable repeaters and microwave amplifier circuits for telephone systems. During World War II he concentrated on the development of radar receivers. After the war he turned to electron tube development and designed the microwave tube, which is the heart of the transcontinental radio relay system for telephone and television transmission.

In 1948 he took charge of all development work on semiconductor devices, especially the transistor. In 1952 he became assistant director of electronic apparatus development, including the transistor and related developments, and in 1953 he was named director of transistor development. In assuming the post of director of device development in 1955, he became responsible for the fundamental development and development for manufacture of electron tubes, solid state devices, and electromechanical and passive devices.

He has been awarded the honorary

(Continued on page 46A)

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For these creative and responsible assignments, we need high caliber men whose salaries will range from \$9,000 to \$15,000.

WRITE TO: William Spangler, Manager—Professional Employment
Department P-12, The Martin Company
Baltimore 3, Maryland

MARTIN
BALTIMORE



This is how a 60' Ruggedized Kennedy antenna looks during a test erection prior to shipment. Erection requires no special tools, is speeded up by functional design and sectionalized construction.



ANTENNA... GOING UP!

No matter which way you look at it, this new 60' Ruggedized Kennedy antenna, slated for service in the northern latitudes, is a real cold-weather performer.

The all-steel reflector is capable of operating when loaded with ice in winds as powerful as a violent hurricane. Yet its simple, functional design and sectionalized construction permit assembly and erection with standard tools at sub-zero temperatures. Its weight is just half that of present steel antennas of comparable size, minimizing shipping problems. Spare parts requirements are simplified, since all like sections are interchangeable. And its galvanized steel construction limits maintenance mainly to routine inspection.

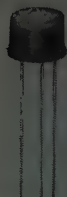


ANTENNA EQUIPMENT

• **D. S. KENNEDY & CO.**

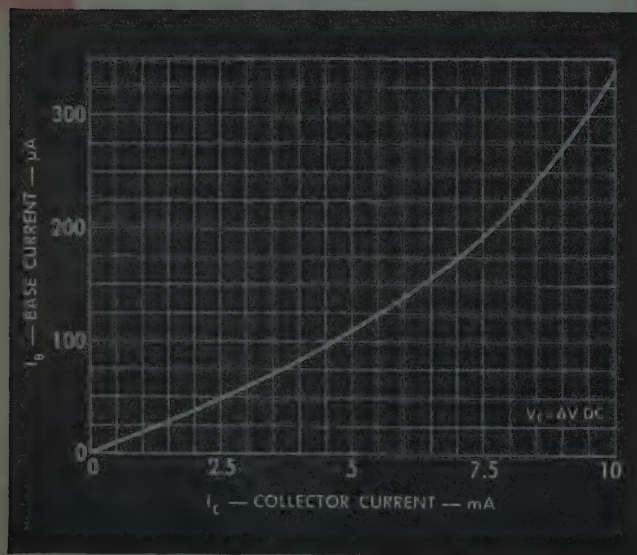
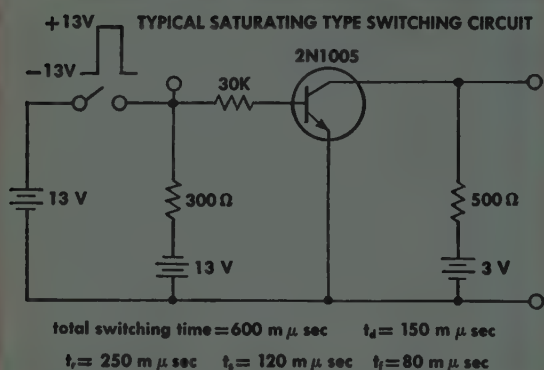
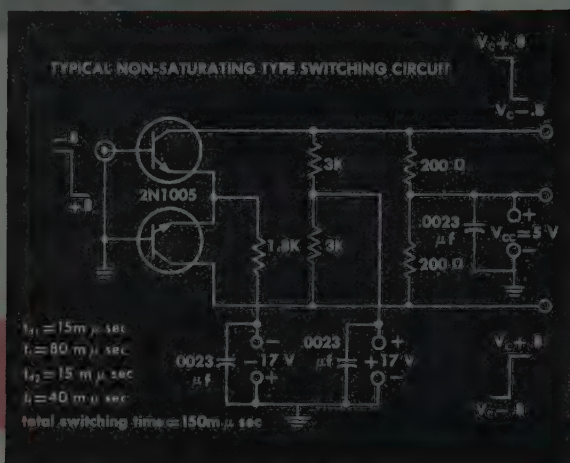
Route 3A, Cohasset, Mass. EVergreen 3-1200

West Coast Affiliate...



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Actual Size



**extremely high speed
switching times as
low as 150 m } \mu \text{ secs}**

**NOW switching times as low as 150 m } \mu \text{ sec with
NEW production-quantity TI 2N1005 and 2N1006
N-P-N silicon transistors!**

The newest additions to the nation's widest transistor line are packaged in the industry preferred JETTER TO-5 package... and *guarantee* DC betas of 20-to-45 and 45-to-100. For the reliability your high speed switching circuits require, both units also *guarantee* h_{fe} greater than 1 at 50 mc, collector dissipation 125 mW at 25°C, 60 ohms saturation resistance, and 0.1 μ A collector cutoff current.

For reliability... plus production quantities delivered on time... select the silicon switchers most suited to your specific applications from the table shown below.

SAME-DAY DELIVERY

FROM YOUR NEARBY TI DISTRIBUTOR

IN 1-249 QUANTITIES

Type	Dissipation at 25°C W	Small Signal Current Transfer Ratio h_{fe} min max	Collector Current I_c mA max	DC Current Transfer Ratio h_{FE} min max	Collector Breakdown Voltage-V BV_{CEO} min	Saturation Resistance R_{CS} Ohms max	Alpha Cutoff Frequency f_{α} mc min
2N337	0.125	19	20	20 55	45	150	10
2N338	0.125	39	20	45 150	45	150	20
* 2N1005	0.125	1 @ 50MC		20 55	15	60	75 (typ)
* 2N1006	0.125	1 @ 50MC		45 150	15	60	75 (typ)

* NEW TYPE ADDED TO PRODUCT LINE

IMMEDIATELY AVAILABLE IN PRODUCTION QUANTITIES

TEXAS



WORLD'S LARGEST SEMICONDUCTOR PLANT



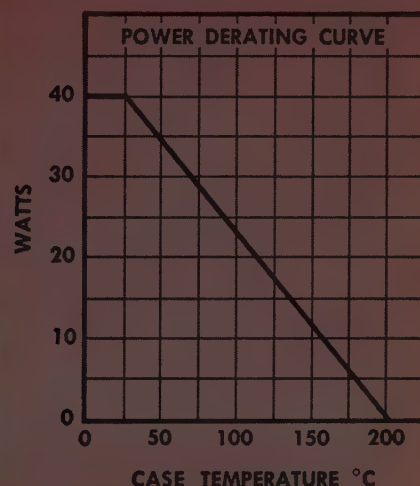
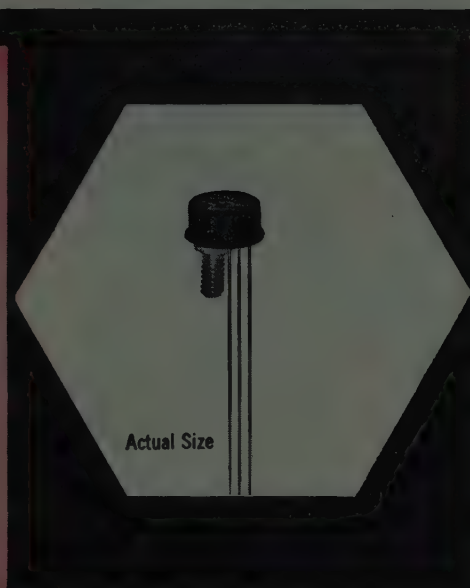
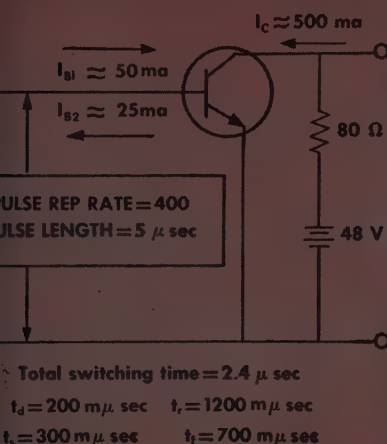
FROM TEXAS INSTRUMENTS!

Intermediate power transistors

0 and 120 BV_{CEX} 2.4 μsec switching

0 W at 100°C operation to 200°C

AL SATURATING TYPE SWITCHING CIRCUIT



TI silicon intermediate power transistors have bridged the gap between high and medium power devices... TI 2N1047, 2N1048, 2N1049, and 2N1050 guarantee 20 watts at 100°C.

For your power switching applications, these latest gaseous diffused transistors provide a typical switching time of 2.4 μsec ! All four new units dissipate 40 watts at 25°C with an infinite heat sink

... the new TI design permits mounting of the semiconductor wafer directly onto the stud.

For your intermediate power and power switching applications, specify the 120-volt 2N1048 and 2N1050 or the 80-volt 2N1047 and 2N1049 with design flexibility and tight beta spreads of 12-to-36 or 30-to-90 that are *guaranteed!*

TI Silicon—Medium Power—Intermediate Power—Power—Transistors

	Type	Dissipation at 25°C W	h _{FE} Typical	I _C mA max	h _{FE}		BV _{CBO} min	R _{CS} Ohms max
					min	max		
Low Power	2N497	4	9 @ 2MC	200	12	36	60	25
	2N498	4	9 @ 2MC	200	12	36	100	25
	2N656	4	6 @ 2MC	200	30	90	60	25
	2N657	4	6 @ 2MC	200	30	90	100	25
Intermediate Power	2N1047	8.75	10 @ 1MC	140	3		120	200
	* 2N1047	40	10 @ 1MC	500	12	36	80	15
	* 2N1048	40	10 @ 1MC	500	12	36	120	15
	* 2N1049	40	9 @ 1MC	500	30	90	80	15
	* 2N1050	40	9 @ 1MC	500	30	90	120	15
Power	2N389	85 at 25°C 45 at 100°C	8.5 @ 1MC	2A	12	60	60	5
	2N424	85 at 25°C 45 at 100°C	6 @ 1MC	2A	12	60	80	10

NEW TYPE ADDED TO PRODUCT LINE

TEXAS INSTRUMENTS
CORPORATED
CONDUCTOR - COMPONENTS DIVISION
N. CENTRAL EXPRESSWAY

TEXAS INSTRUMENTS SALES OFFICES
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MAGNETICS RESEARCH • NARDA MICROWAVE • NJE • SYSTRON
WAYNE-KERR LABORATORIES.

**Miss Grayner is turning on the heat. One of our customers needs better-than-promised delivery on an instrument, and she is talking directly to the factory production manager, who works three or four such miracles every month for her. Her phone bills are astronomical, but our customers get the hardware...when they need it. One more reason to "Get the Product from the Heart".*



IRE People



(Continued from page 42A)

Doctor of Science degree by Ohio State University (1954) and his alma mater, Wayne University (1956). In 1948 he received an honorable mention award from Eta Kappa Nu, and in 1951 a University Alumni Award from Wayne University for "distinguished service and accomplishment in science." In 1953, at the University of Michigan Centennial, he was cited for his contributions to science.

Mr. Morton is the author of numerous technical articles and reports and has served on many technical committees. He is a member of the American Institute of Electrical Engineers, Eta Kappa Nu, Phi Kappa Phi, Sigma Xi, and the McKenzie Honor Society.



Meyer Leifer (A'46-M'48-SM'50-F'55) has been appointed manager of special tube operations for Sylvania Electric Products Inc. He has held managerial posts for Sylvania on the West Coast for the past five years. In his new post he will be responsible for directing an "expanding program of research, development and production in the microwave field," including special tube and component work. Included in his organization will be production facilities at Mountain View and Williamsport, Pa., and the Microwave Tube and Microwave Physics Laboratories which have been grouped into the Microwave Components Laboratories in Mountain View.



M. LEIFER

Prior to his new appointment he was manager of the Microwave Tube Laboratory in Mountain View. He joined Sylvania in 1946 as an engineer in Sylvania's Physics Laboratory in Bayside, N. Y., becoming manager of the systems and circuits branch in 1951. In 1953, he was instrumental in establishing the Electronic Defense Laboratory, becoming its engineering manager and, in 1956, its assistant director. He was named manager of the Microwave Tube Laboratory in 1957.

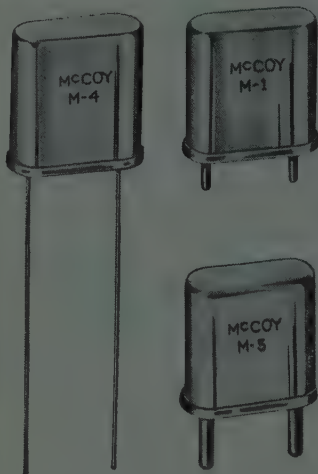
His previous experience includes positions with the Bureau of Labor Statistics, the National Advisory Committee for Aeronautics, and teaching high school in New York. During World War II, he served as a physicist with the United States Navy, specializing in degaussing—a technique of treating ships electrically to protect them from magnetic mines—and as a Naval officer in the Pacific Theater.

A graduate of Brooklyn College with the B.S. degree in mathematics, Mr. Leifer also holds a master's degree in physics from Columbia University, and has completed all course requirements for a

(Continued on page 48A)

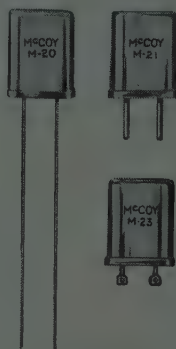
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Regardless of size,
weight, or shape,
a McCoy crystal will
deliver the
utmost in stability
under extreme
conditions of
shock and
vibration.

Frequency range
of M-1, M-4 and M-5;
200 kc. to 200 mc.
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IRE People

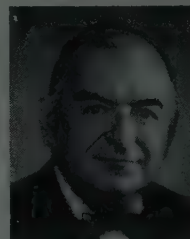


(Continued from page 46A)

doctorate from New York University. He is a past chairman of the IRE's San Francisco Section, past president of the Sequoia branch of the Research Society of America, and a member of the American Physical Society, Pi Mu Epsilon, Sigma Pi Sigma, and Sigma Xi.



Frederick R. Lack (A'20-F'37), noted electronics engineer and executive, has been elected a director of Hazeltine Corporation, Little Neck, Long Island, N. Y., it was announced by Philip F. LaFollette, president.



F. R. LACK

Dr. Lack retired in August as a director and vice-president of the Western Electric Company, in which capacity he had served since 1942, having been with Western Electric since 1911.

The Hazeltine Corporation has been a leader in the electronics field since 1924. It has functioned as prime contractor and systems manager, as well as subcontractor, for government electronics projects including SAGE, IFF (Identification Friend or Foe), and various radar programs. The company also holds numerous basic patents in the fields of commercial radio, television and color television.

A Lieutenant in the Signal Corps in France, 1917-1919, Dr. Lack earned the B.S. degree at Harvard University in 1925, and was given the honorary degree of Doctor of Science by Albright College, Reading, Pa., in 1958. During World War II he served in Washington as director of the Army and Navy Electronics Production Agency, and later was chairman of the Joint Electronics Industry Committee. A pioneer in radio telephony, he was in charge of designing and building the first commercial ship-to-shore radio telephone, installed on S. S. Leviathan.

He helped to build up the Electronics Industry Association, of which he was a director. He was also a director of the Armed Forces Communications and Electronics Association, and on the Executive Committee of the National Security Industrial Association. Interested also in education, he has been on the visitors' committee for the Board of Overseers of Harvard College, a national sponsor for the Harvard Foundation for Advanced Study and Research, and president of the Harvard Engineering Society.

He is a Fellow of the American Institute of Electrical Engineers and the American Association for the Advancement of Science, and a member of the American Physical Society.



(Continued on page 50A)



Another new miniature from Corning...

1 to 8 uufd direct traverse trimmer capacitor

Small but still precise, this new Corning direct traverse type trimmer capacitor meets military as well as civilian requirements.

Other features besides its size:

Silver plated hardware takes the noise out of tuning and protects the unit from corrosion even under extreme environments.

Mechanical stops at both ends of capacitance adjustment, with self-contained adjusting shaft.

Linear tuning with fine resolution. About 0.50 uufd capacitance change per turn.

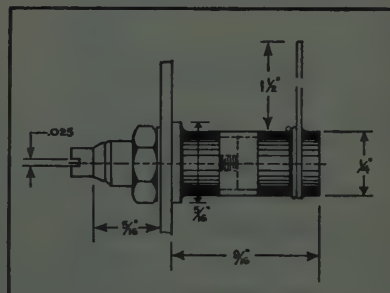
No capacitance reversals.

Glass-Invar construction.

Bushing and shaft assembly is coaxial for low inductance, high frequency applications.

Shock, vibration, and thermal shock resistance all excellent.

If you'd like more information, write for our new data sheet.



Corning means research in Glass



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The further we progress,
the more important
experience becomes in solving
today's most urgent problems.



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engaged in advanced ECM research
and development
since 1952 is ...

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Advanced Home Study and Residence
Courses in Practical Electronics Automation
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3224 16th St., N. W. Washington 10, D. C.

Approved for Veteran Training



IRE People



(Continued from page 48A)

Stewart Nellis (A'57) has been named sales manager of Technical Wire Products, Inc., Springfield, N. J., according to an announcement by Ralf L. Hartwell, president.

Mr. Nellis has had a wide background in the field of electronics, particularly radio interference. He was previously sales and development engineer for a producer of wire cloth products, and did work in radio interference with the Materials Laboratory of the New York Naval Shipyard, Brooklyn, N. Y.

He is a native of New York and was graduated from New York University. He is a charter member of the Professional Group on Radio Interference and is a member of the Newsletter Committee of the Group.



S. NELLIS

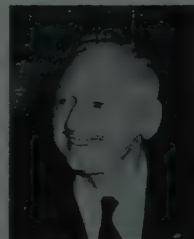
Robert Adams (M'57) has been named manager of eastern operations for Packard-Bell Electronics Corporation, with headquarters in Washington, D. C. He assumes the duties of Commodore A. J. Spriggs, USN (ret.) (SM'47), Packard-Bell vice-president now on loan to the U. S. Department of Commerce as advisor to the director, Electronics Division.

A graduate of Drexel Institute of Technology, Philadelphia, Pa., where he received the B.S.E.E. degree, Mr. Adams served for fifteen years in the armed forces, as a communications officer in the U. S. Naval Reserve and during World War II as a U. S. Signal Corps contracting officer, with rank of major, at Wright Air Development Center and Fort Monmouth.

His business background spans 30 years as an executive in engineering, manufacturing, and sales for major eastern and mid-western electronics firms, including Stewart-Warner, Oxford Electric Corp., Bendix Radio, Sterling Precision Corp., RCA, and General Electric. He comes to Packard-Bell from The Hallicrafters Co., Chicago, Ill., where he was East Coast military representative.

Active since 1919 in amateur radio (present call, W3SW), Mr. Adams writes a monthly column on single sideband for the magazine CQ.

(Continued on page 52A)



R. ADAMS

Use your
IRE DIRECTORY!
It's valuable!

*for regulating...
limiting...
clipping...*

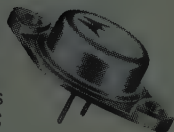
MOTOROLA ZENER DIODES

10 AND 50 WATT TYPES
UP TO 200 VOLTS

10WZ
SERIES
10 watts
@ 55°C



50WZ
SERIES
50 watts
@ 55°C



TYPICAL APPLICATIONS

- Regulation of DC voltage
- DC level changing and coupling
- Surge protection
- Regulation of vacuum tube heaters
- Arc suppression
- Wherever a constant DC voltage independent of current is desired.

- Very high power ratings... both 50 and 10 watt types available.
- Wide voltage range... up to 200 volts in both series.
- Very low Zener impedance limits.
- "Soft" or unstable Zener knees eliminated... by impedance limits at 5 mA for 50 watt types, at 1 mA for 10 watt types.
- Controlled forward characteristics... for applications requiring conduction in both directions.
- Available with either anode or cathode connected to case.
- Conservatively rated... excellent long-time stability.
- Designed for military usage.
- Operating and storage temperature range -65°C to +175°C.
- Standard packages
 - 10 WATT TYPES in welded, hermetically sealed, metal to glass, Jetec package.
 - 50 WATT TYPES in plug-in or solder-in TO-3 package with .052 inch diameter pins and series interlock construction for protection against overvoltage on load.
- Various tolerance ranges available. Inquiries invited on AC clippers and on your special requirements.

*for complete
technical information*

concerning Motorola Zener Regulators, contact the nearest Motorola regional office listed below or...

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BRidge 5-4411 • Teletype Px80



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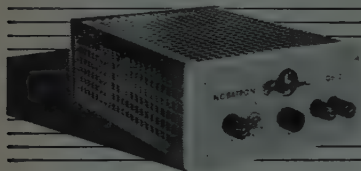
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NEW IDEAS IN PACKAGED POWER

for lab, production test,
test maintenance, or as a
component or subsystem
in your own products



0.01% regulation—Why be half safe?
You can get a-c line voltage regulation to the exact degree of precision you need from Sorensen. Model 2501 (left) regulates a-c line voltage to $\pm 0.01\%$ at 2500 VA. Other Sorensen a-c models range in precision from meter calibrators to rugged "constant voltage transformers," designed to give you maximum volt-amps per dollar.



Fully-transistorized regulated d-c supplies—The most complete line of transistorized low-voltage d-c power supplies on the market—like the new Model Q6-2 (left)—is offered by Sorensen. Regulation accuracy is $\pm 0.25\%$ (line and load combined). Life is exceptional. Response speed is extremely fast. They come with voltage adjustable over 2:1 range (Model Q Series) in 6, 12, 28 vdc and capacities to 200 watts. Also in 0-36, or 0-75 vdc continuously variable "Rangers" (Model QR Series) of 150-watt capacity.



Here's a d-c workhorse for rack-panel equipment—New Sorensen Model MD supplies feature magnetic regulation, semiconductor rectifiers, capacitance-input filters—and low cost. What's more you get any factory preset voltage you want, from 2.5 vdc to 1000 vdc. Available in 8 sizes from 25 to 3000 watts. No switches, no fuses (short circuited output is not recommended, but is not damaging). Ideal for powering your 19" rack-panel equipment.

Sorensen has many other ideas for packaging power to your needs, including standard off-the-shelf models, both electronic and transistorized, to take care of almost every need for controlled power—whether ac or dc, low or high voltage, low or high current. Ask for the latest Sorensen catalog. And let Sorensen engineers talk over with you a complete power system for your complex electronic equipment.



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**WIDEST LINE OF CONTROLLED-POWER
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IN EUROPE, contact Sorensen-Ardag, Zurich, Switzerland. IN WESTERN CANADA, ARVA.
IN EASTERN CANADA, Bayly Engineering, Ltd. IN MEXICO, Electro Labs, S. A., Mexico City.



IRE People



(Continued from page 50A)

The Massachusetts Institute of Technology has announced the appointment of **Dr. Claude E. Shannon** (S'36-M'48-SM'49-F'50) to the recently established Donner Chair of Science.



C. E. SHANNON

The new professorship was made possible by a \$500,000 grant from the Donner Foundation of Philadelphia. Dr. Shannon is a mathematician, an electrical engineer, and a leader in the new field of information theory. He is Professor of Communications Sciences in the Department of Electrical Engineering and Professor of Mathematics.



Dr. Alfred N. Goldsmith (IRE Charter Mem.) (M'12-F'15) (L), consulting engineer in the electronics and motion picture fields, has been elected to the Board of Directors of RCA Communications, Inc., it has been announced by David Sarnoff, Chairman of the Board of RCA and RCA Communications, Inc.



A. N. GOLDSMITH

Dr. Goldsmith joined RCA in 1919, and for 12 years served as director of research and then as vice-president and general engineer. Since 1931 he has served as a technical consultant to RCA.

He has been president of the IRE and of the Society of Motion Picture and Television Engineers. He is a Fellow of the AIEE, the American Physical Society, the American Association for the Advancement of Science, the Acoustical Society of America, the Optical Society of America, and the International College of Surgeons.

Among the citations he has received are the Medal of Honor and Founders Awards of the IRE, the Progress Medal Award of the Society of Motion Picture and Television Engineers, and the Modern Pioneers Award.

Prior to his association with RCA, Dr. Goldsmith was a member of the teaching staff of City College of New York and technical director of the Naval Radio Compass School and the Signal Corps Radio School. From 1917 to 1919 he was director of research for the Marconi Wireless Telegraph Company of America.

He holds the degrees of B.S. (C.C.N.Y.), Ph.D. (Columbia University, New York, N. Y.), and D.Sc. Hon. (Lawrence College, Appleton, Wis.).



(Continued on page 54A)

A **NEW** POWER FERRITE for FLYBACK TRANSFORMERS by ALLEN-BRADLEY



**HIGHER FLUX DENSITY
LOWER CORE LOSSES
HIGHER CURIE POINT**

Now, with the higher flux density of Allen-Bradley's new Class W-04 ferrite, you can design smaller flyback transformers with smaller cores. This saves space . . . saves weight . . . and saves copper, too. And the new ferrite is priced so that, with this smaller size, the actual cost of the core itself is also reduced.

Specify Allen-Bradley's new W-04 ferrite for *your* flyback transformers. The table on the following page compares the superior characteristics of the new W-04 with Allen-Bradley's "premium quality" W-03 ferrite.

ALLEN-BRADLEY CO.
ELECTRONIC COMPONENTS

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Check the

superior characteristics
of this

NEW ALLEN-BRADLEY W-04 Power Ferrite

Class	Temp. °C	B_{\max}^* in Gauss at 10 Oe	Core Loss P_h in $\frac{\mu\text{Watts}}{\text{cm}^3\text{cps}}$				μ_{\max}^*	μ_0 at Room Temp.	B_u^{**}	μ at B_u †	Curie Temp. °C
			B=1350 Gauss		B=1800 Gauss						
			16 Kcps	60 Kcps	16 Kcps	60 Kcps					

RECOMMENDED FOR FLYBACK TRANSFORMER CORES (AND OTHER POWER APPLICATIONS)

W-04	25	4900 ± 10%	3.8 ± 20%	5.3 ± 20%	6.4 ± 20%	9.0 ± 20%	7000 ± 30%	2000	2700 ± 15%	6000 ± 25%	225
	115	3700 ± 10%	3.8 ± 20%	5.3 ± 20%	6.4 ± 20%	9.0 ± 20%	7000 ± 30%				
W-03	25	4200 ± 10%	4.1 ± 20%	5.5 ± 20%	6.9 ± 20%	9.1 ± 20%	6000 ± 30%	2000	2100 ± 15%	5600 ± 25%	180
	115	2800 ± 10%	4.2 ± 20%	6.5 ± 20%	6.9 ± 20%	10.0 ± 20%	6000 ± 30%				

RECOMMENDED FOR TV YOKE CORES

W-01	25	2850 ± 10%	5.8 ± 30%	9.5 ± 30%	9.2 ± 30%	16.0 ± 30%	5000 ± 20%	850	1200 ± 20%	5000 ± 25%	180
	115	2000 ± 10%	4.4 ± 30%	7.9 ± 30%	7.4 ± 30%	14.5 ± 30%	6000 ± 30%				

* B_{max} and μ_{max} , Frequency—16 Kcps.

**Usable flux density—flux density at which the 115°C permeability is equal to ½ of the 25°C permeability.

†Permeability of the core at 25°C at B_u .

The above table shows the superiority of the new W-04 ferrite—higher flux density, higher permeability, lower core loss . . . properties that permit significant improvement in your flyback transformer design.

Allen-Bradley has also developed new square-loop power ferrites (R-03), and ferrites with unique characteristics for transistorized medium frequency power inverters (W-07).

The experienced engineering staff at Allen-Bradley will be glad to assist you with your ferrite problems. Write, today!

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222 W. Greenfield Ave., Milwaukee 4, Wis.
In Canada—
Allen-Bradley Canada Ltd., Galt, Ont.



ALLEN-BRADLEY CO.
ELECTRONIC COMPONENTS

Allen-Bradley ferrites are available in a wide range of shapes and sizes for various applications. Just a few of the basic shapes and sizes are shown above.



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SYSTEMS MANAGEMENT*

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Firm central control...

over interlocking functions of
Engineering and Finance...

under a member of
top management whose
authority is undiluted—

this, the Stromberg-Carlson
concept of Systems Management,
is a definite departure from
conventional methods.

It's working extremely well.

Unified direction of all our own
divisions, leading consultants
and qualified subcontractors
assures a tight control of costs
and more efficient utilization
of facilities.

Currently, this concept is
helping develop an electronic
countermeasures system vital to
the defense of the free world.

Our talent is equally
applicable to
Communication,
Navigation, Test
Equipment and
other complex
electronic systems.
Our brochure 709
would be of interest.



For DEPENDABILITY

USE HICKORY BRAND

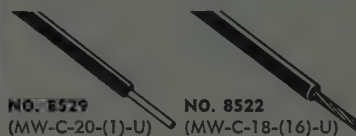


ELECTRONIC WIRES and CABLES

- QUALITY-ENGINEERED
- PRECISION-MANUFACTURED
- PLASTIC INSULATED AND SHEATHED

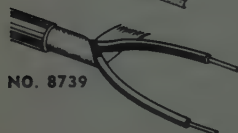
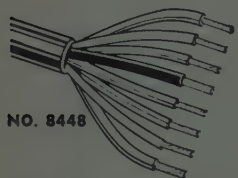
MW HOOKUP WIRE

Use for electronic devices, aircraft instruments, radio and radar transmitters, receivers, lighting and power rectifiers. Thirty color combinations. Features high dielectric strength, resistance to acids, alkalis, oil, flame and moisture. Fungus-proof. Temperature rating minus 40° to 80° C.



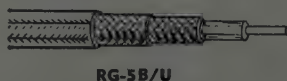
INTERCOMMUNICATING and SOUND SYSTEM CABLES

Shielded and unshielded cables available, also composite types. Designed for long service life, excellent mechanical and electrical characteristics. Use for balanced intercom systems, annunciators, telephones, control circuit cable, electronic computer cable, multiple speaker and signal systems.



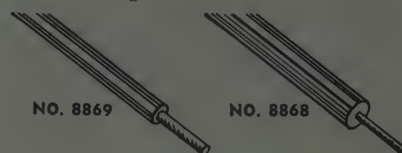
COAXIAL CABLES

Maximum operating efficiency in applications requiring high, very high and ultra-high frequencies.



HOOKUP and LEAD WIRES

Use for high voltage leads to cathode ray tubes. Features high dielectric strength, corona resistance and minimum surface leakage.



Write for complete information on
the full line of HICKORY BRAND
Electronic Wires and Cables

HICKORY BRAND Electronic Wires and Cables

Manufactured by
SUPERIOR CABLE CORPORATION, Hickory, North Carolina



IRE People

(Continued from page 52A)

Beatrice A. Hicks (S'42-A'44-M'51-SM'57), president of Newark Controls Co., Bloomfield, N. J., received the honorary degree of Doctor of Science at a special convocation of Hobart and William Smith Colleges, Geneva, N. Y., which was called to celebrate the 50th anniversary of William Smith College. In presenting the degree, President Hirshson said in part: "You, as scientist, engineer and executive, have pioneered in areas of research and accomplishment unpredictable a century ago." Participating in a panel program concerning the relationship of college to career, home, and society, she spoke particularly on careers and the education required.



B. A. Hicks

Miss Hicks, a past president of the Society of Women Engineers, is affiliated with many technical societies and is a registered Professional Engineer in New York and New Jersey. She is a Senior Member of the American Society of Mechanical Engineers and the American Society of Heating and Air-Conditioning Engineers, and president of the Newark College of Engineering Alumni Association.

The Newark Controls Co. manufactures electromechanical controls and has done a great deal of pioneer work in pressure and gas density sensing for aircraft and missiles.

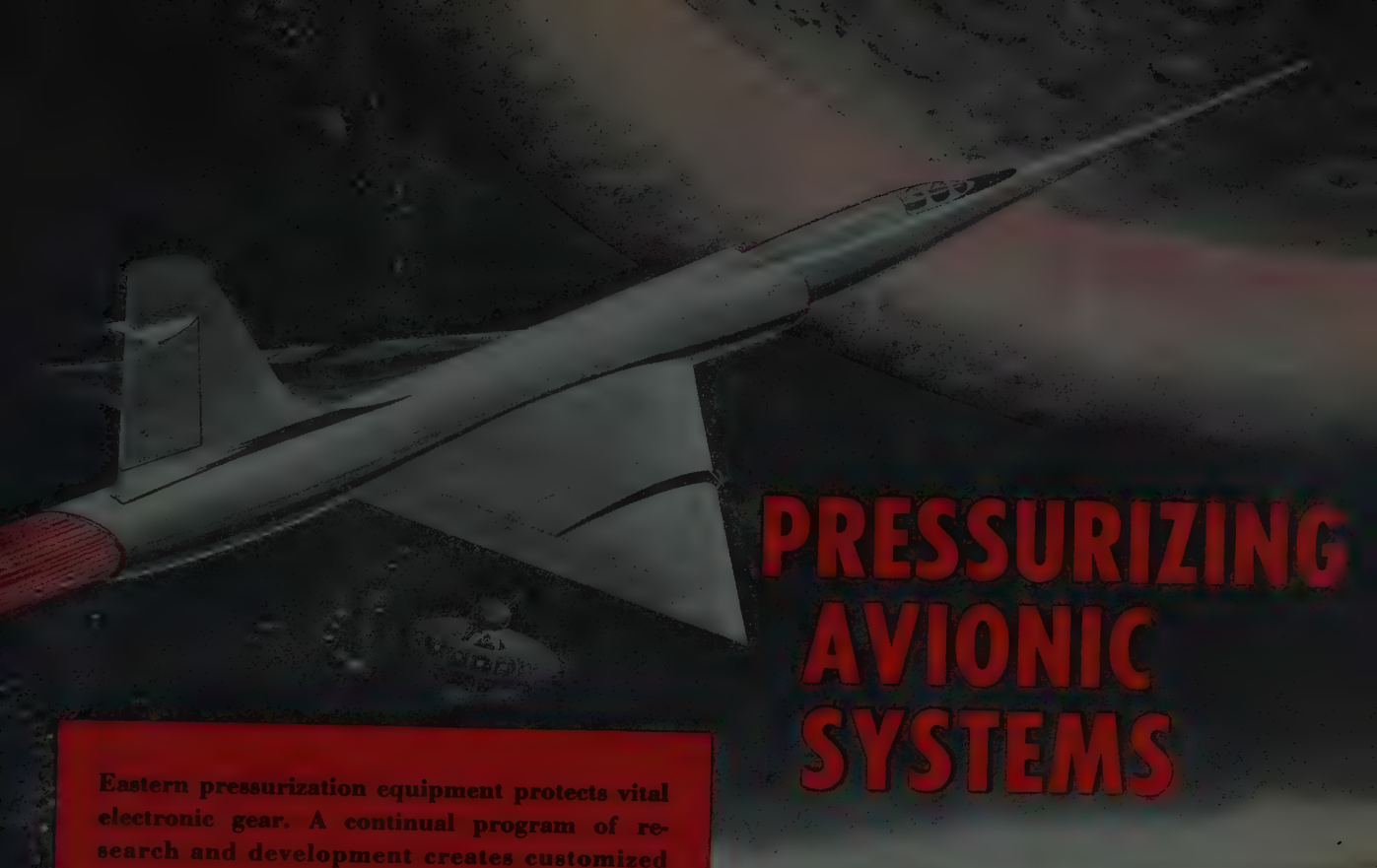
William S. Aiken (A'55-SM'57) has been named manager of the project engineering department and acting manager of the programming department of the engineering division of the Thompson-Ramo-Wooldridge Products Co., Los Angeles, Calif. The company is jointly owned by the Ramo-Wooldridge Corp., Los Angeles, and Thompson Products, Inc., Cleveland, Ohio. It specializes in industrial control and data reduction systems incorporating the nation's first digital control computer, the RW-300. The project engineering department handles the installation and check-out of computer control and data logging systems.

Mr. Aiken has extensive experience in electronic design, analog computers, missile systems, controls, instrumentation, flight test, guidance, and radar. For nine years prior to joining Thompson-Ramo-Wooldridge Products in 1957 he was associated with Sperry Gyroscope, Great Neck, Long Island, and Point Mugu.

He was born in New Orleans, La., and received the B.S. degree in physics in 1943 from Yale University and the M.S. degree in physics, electrical engineering, and mathematics in 1948 from M.I.T. He was also a research assistant at M.I.T.

Mr. Aiken is an associate member of Sigma Xi.

(Continued on page 56A)



PRESSURIZING AVIONIC SYSTEMS

Eastern pressurization equipment protects vital electronic gear. A continual program of research and development creates customized pressurization units that keep the performance of avionic systems unaffected by altitude and ambient conditions. Custom units that *meet military specifications* help to solve your problems when recommending electronic components.

When you have a challenging problem to prevent pressure, or heat, or moisture, or dust from affecting electronic performance, come to Eastern for complete and creative engineering help.



1500 SERIES
PRESSURIZATION UNIT



100 SERIES
PRESSURIZATION UNIT

EASTERN PRESSURIZATION UNITS

A variety of capacities accommodates a broad range of requirements and meets appropriate government standards. Typical units operate from zero to over 70,000 feet at temperatures from -65°F to $+160^{\circ}\text{F}$. Delivery: 0-3600 cu. in./min. free delivery, Discharge Pressure: 0-60 p.s.i. Standard sub-assemblies and components normally are used to create a custom-made design to fit your exact needs. Units may consist of an air pump and motor assembly, pressure switch, check valve, tank valve, terminal connectors, and dehydrator.

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*Gives you direct
capacitance reading
from 0.01 μf to 12 μf*

**BALLANTINE
CAPACITANCE
METER
Model 520**



The Model 520 Capacitance Meter is a general laboratory instrument which measures capacitance over the wide range found in paper, plastic, mica, ceramic and air type capacitors. The value of unknown capacitance is read directly from the meter scale by manipulating only one control knob. The ability to measure direct capacitance, excluding strays, makes it very useful for low value measurements. Adjustable limit pointers, together with fast operation, make it valuable for incoming inspection departments. The instrument has a built-in calibration standard.

SPECIFICATIONS

RANGE: 0.01 μf to 12 μf	FREQUENCY: 1,000 cps
ACCURACY: 2%, 0.1 μf to 12 μf ;	METER: Logarithmic scale
5%, 0.01 μf to 0.1 μf	SIZE: 13½" x 7½" x 7"

BALLANTINE LABORATORIES, INC.



Boonton, New Jersey



IRE People



(Continued from page 54A)

Peter D. Strum (A'45-SM'55) has been named co-receiver of the Annual Award of the National Electronics Conference for the best technical paper presented at the 1957 conference. Announcement of the award was made at the opening of the 1958 conference in Chicago in October. The title of the winning paper, which Mr. Strum co-authored with Dr. J. W. Meyer and Dr. A. L. McWhorter (S'51-M'56) of M.I.T.'s Lincoln Laboratory in Lexington, Mass., was "Noise Temperature Measurement of a Solid-State Maser."

Mr. Strum recently left General Radio Co., Cambridge, Mass., to join Granger Associates, Palo Alto, Calif., as supervisory engineer. His previous positions were vice-president for engineering of Ewen-Knight Corp., Needham, Mass.; chief engineer of the receiver department of National Co., Malden, Mass.; and assistant supervisory engineer at Airborne Instruments Lab., Mineola, N. Y. His major professional fields are VHF and microwave receivers and radio astronomy.

He received the B.S. degree from North Carolina State College and the M.S. degree in engineering from Stanford University. He is a native of Brunswick County, Va.

Last year Mr. Strum was chairman of the Boston chapter of the IRE Professional Group on Microwave Theory and Techniques. He is a member of the national administrative committee and editorial board of the PGMTT.



Brigadier General Francis F. Uhrhane, USA (SM'55) was the principal speaker at a luncheon held during the Fourth National Aero-Com Symposium. The Symposium was conducted by the Rome-Utica Section of the IRE in the Rome-Utica area from October 20-22. General Uhrhane, who is Deputy Chief of Staff for Communications and Electronics of NORAD

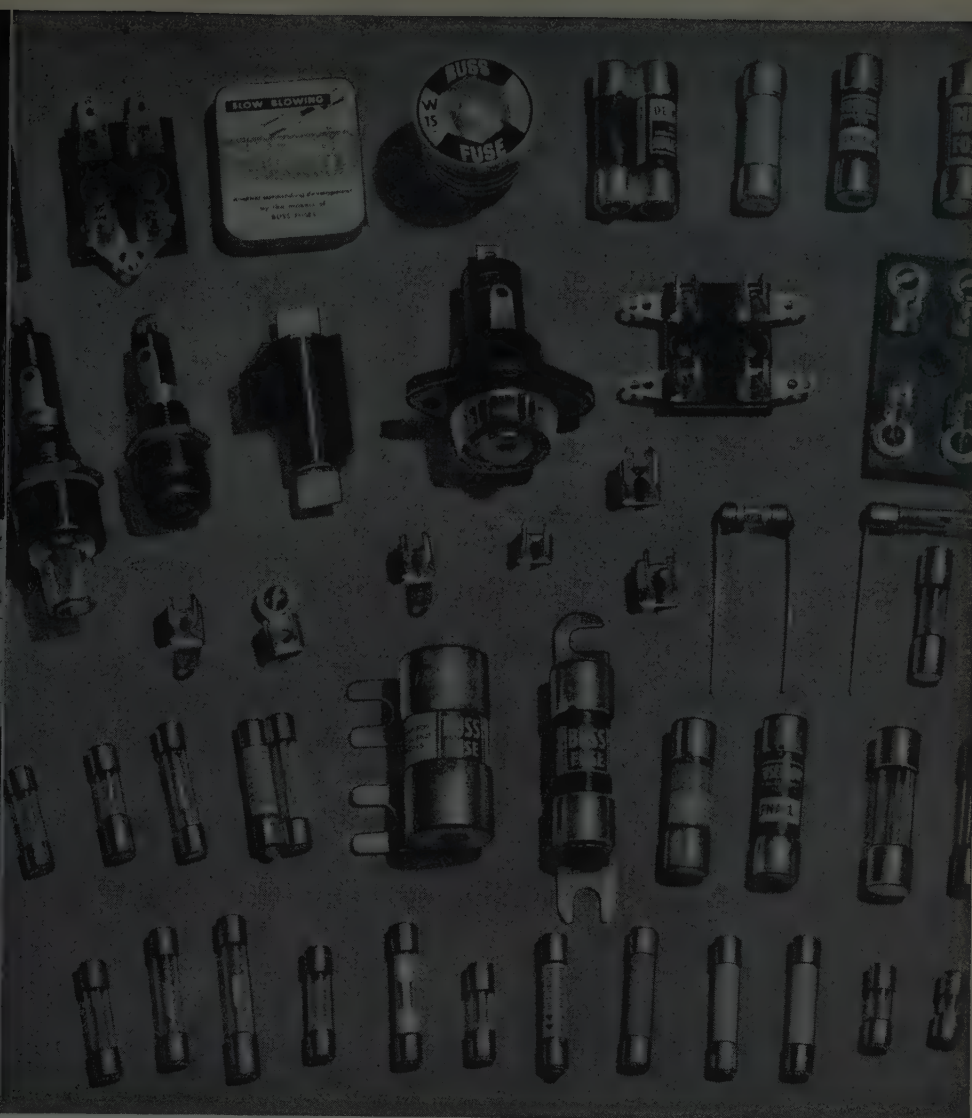
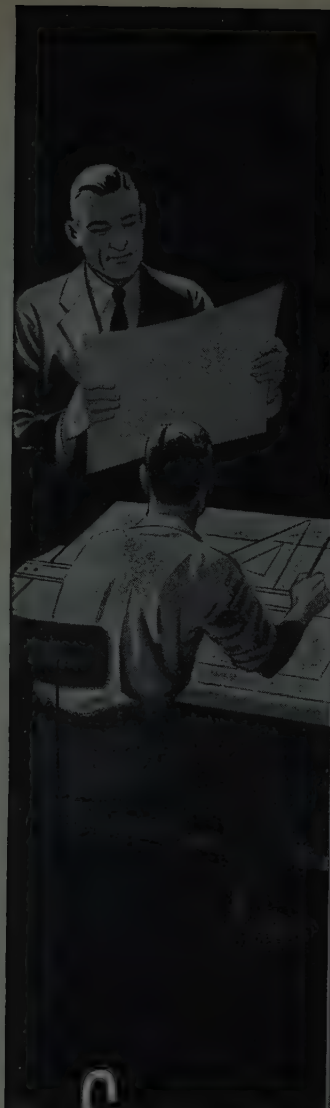


F. F. UHRHANE

(North American Defense Command), spoke on the subject of "NORAD and Its Communications Problems." He discussed the vital role played by communications and electronics in the defense of the North American continent, the problems encountered in providing the necessary communications facilities, solutions to these problems, and the vital role of air defense in general and some of its ramifications.

(Continued on page 58A)

**Use your
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It's valuable!**



Guard against needless trouble and shutdowns ... by specifying dependable *BUSS* fuses!

Should a fuse fail to protect your equipment if electrical trouble occurs... unnecessary damage results. Or, if a fuse blows needlessly your equipment is shutdown without good cause.

Why risk faulty fuses causing trouble and reflecting on the service and reliability of your equipment? You can be sure of dependable electrical protection by specifying *BUSS* fuses.

Every *BUSS* fuse is tested in a sensitive electronic device that automatically rejects any fuse not cor-

rectly calibrated, properly constructed and right in all physical dimensions.

One source for all your fuse needs.

To meet your needs, — the *BUSS* line of fuses is most complete... plus a companion line of fuse clips, blocks and holders.

To help you on special problems in electrical protection...

... *BUSS* places at your service the facilities of the world's largest fuse research laboratory and its staff of engineers. If possible, our

engineers will help you select a fuse readily available in local wholesalers' stocks so users can easily obtain fuses for replacement.

For more information on the complete line of *BUSS* and *FUSETRON* Small Dimension Fuses and Fuse-holders, write for bulletin SFB.

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BUSS fuses are made to protect — not to blow, needlessly



BUSS MAKES A COMPLETE LINE OF FUSES FOR HOME, FARM, COMMERCIAL, ELECTRONIC, AUTOMOTIVE AND INDUSTRIAL USE.

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FILAMENT, PULSE
& AUDIO TRANSFORMERS

FOR IMMEDIATE
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POWER TRANSFORMERS-STANDARD

All primaries 105/115/125 v., 60 cps.

Cat. No.	HI Volt Sec.	ct	DC Volts	DC Amps	Filament		MIL Case Size
					#1	#2	
MGP1	400/200	✓	185	.070	6.3/5	2 6.3	3 HA
MGP2	650	✓	260	.070	6.3/5	2 6.3	4 JB
MGP3	650	✓	245	.150	6.3	5 5.0	3 KB
MGP4	800	✓	318	.175	5.0	3 6.3	8 LB
MGP5	900	✓	345	.250	5.0	3 6.3	8 MB
MGP6	700	✓	255	.250			KB
MGP7	1100	✓	419	.250			LB
MGP8	1600	✓	640	.250			NB

FILAMENT TRANSFORMERS-STANDARD

All primaries 105/115/125 v., 60 cps.

Cat. No.	Secondary		Test VRMS	MIL Case
	Volt	Amp		
MGF1	2.5	3.0	2,500	EB
MGF2	2.5	10.0	2,500	GB
MGF3	5.0	3.0	2,500	FB
MGF4	5.0	10.0	2,500	HB
MGF5	6.3	2.0	2,500	FB
MGF6	6.3	5.0	2,500	GB
MGF7	6.3	10.0	2,500	JB
MGF8	6.3	20.0	2,500	KB
MGF9	2.5	10.0	10,000	JB
MGF10	5.0	10.0	10,000	KB

PULSE TRANSFORMERS

Cat. No.	Block, Sec.	Int. Coupling	Low Pow. Out.	Pulse Voltage Microvolts	Pulse Duration Microseconds	Duty Rate	No. of Wdg.	Test Volt. KV RMS	Char. Imp. Ohms
MPT1	✓	✓	0.25/0.25/0.25	0.2-1.0	.004	3	0.7	250	
MPT2	✓	✓	0.25/0.25	0.2-1.0	.004	2	0.7	250	
MPT3	✓	✓	0.5/0.5/0.5	0.2-1.5	.002	3	1.0	250	
MPT4	✓	✓	0.5/0.5	0.2-1.5	.002	2	1.0	250	
MPT5	✓	✓	0.5/0.5/0.5	0.5-2.0	.002	3	1.0	500	
MPT6	✓	✓	0.5/0.5	0.5-2.0	.002	2	1.0	500	
MPT7	✓	✓	0.7/0.7/0.7	0.5-1.5	.002	3	1.5	200	
MPT8	✓	✓	0.7/0.7	0.5-1.5	.002	2	1.5	200	
MPT9	✓	✓	1.0/1.0/1.0	0.7-3.5	.002	3	2.0	200	
MPT10	✓	✓	1.0/1.0	0.7-3.5	.002	2	2.0	200	
MPT11	✓	✓	1.0/1.0/1.0	1.0-5.0	.002	3	2.0	500	
MPT12	✓	✓	0.15/0.15/0.3/0.3	0.2-1.0	.004	4	0.7	700	

AUDIO TRANSFORMERS

Freq. resp. 300 to 10000 cps ± 2 DB. All Case Sizes AJ

Casing No.	Application	Impedance		DC Current	Max. Level
		Prim. Ohms	Sec. Ohms		
MGA1	Single or P.P. Plates — to Single or P.P. Grids	10K	90K Split	✓ 10 10	± 15
MGA2	Line to Voice Coil	600 Split	4, 8, 16	0 0	± 33
MGA3	Line to Single or P.P. Grids	600 Split	135K	✓ 0 0	± 15
MGA4	Line to Line	600 Split	600 Split	0 0	± 15
MGA5	Single Plate to Line	7.6K 4.8T	600 Split	40 40	± 33
MGA6	Single Plate to Voice Coil	7.0K 4.8T	4, 8, 16	40 40	± 33
MGA7	Single or P.P. Plates to Line	15K	600 Split	10 10	± 33
MGA8	P.P. Plates to Line	24K	600 Split	10 1	± 30
MGA9	P.P. Plates to Line	40K	600 Split	10 1	± 27

Write for further information on these units and special designs and complete line of MIL-T-27 Re-actors also available from stock. Send for complete catalog

FREED
TRANSFORMER CO., INC.

1720 Weirfield Street
Brooklyn (Ridgewood) 27, New York



IRE People



(Continued from page 56A)

General Uhrhane was born at Marietta, Ohio, on June 26, 1906. He graduated from the United States Military Academy at West Point with the class of 1930. He received the M.S. degree in communications engineering from The Ohio State University in 1936.

A veteran Army communications officer, the general came to NORAD from the Pentagon in Washington, D. C., where he headed the research and development division in the office of the Chief Signal Officer. During the period July 1953 to May 1955 he commanded the Signal Corps Engineering Laboratories at Fort Monmouth, N. J.

In World War II, General Uhrhane served as director of the technical liaison division for headquarters of the Army in the European Theater of Operations, and was the signal supply officer for the Eighth Army during the Korean hostilities.

He has attended and completed courses of study at the Army Signal Corps School, Fort Monmouth, N. J., and the Armed Forces Industrial College, Fort McNair, Virginia.

For his distinguished performance in Army electronics and logistics, he has received two Legions of Merit and the Bronze Star Medal.

Kenneth G. McKay (M'47-SM'58) has been named director of development of components and solid state devices at Bell Telephone Laboratories. He will head a general department being established as the volume of work in the field of device development at Bell Labs. increases.

He is a native of Montreal, Canada, and a graduate of McGill University, where he received the B.S. and M.S. degrees in 1938 and 1939, respectively. He was awarded the



K. G. McKay

Ph.D. degree by Massachusetts Institute of Technology in 1941, and worked with the National Research Council in Canada for the next five years.

Upon joining Bell Labs. in 1946 he undertook fundamental research studies on the physics of solids, including the interaction of energetic electrons with solids, and studies of secondary electron emission and electron bombardment conductivity in insulators and semiconductors. Later his work related to the electrical and optical characteristics of electrical breakdown in germanium and silicon.

In 1952 he was named to head a group concerned with physical electronics research, and in 1954 he was placed in charge of the solid state research group. He was named director of development of solid state devices in 1957.

He has been granted nine patents for his electronic inventions, and has written extensively on solid state physics for scientific publications.

Dr. McKay is a Fellow of the American Physical Society and served on the board of editors of *The Physical Review* from 1955 to 1957. He is a member of the Research Society of America.

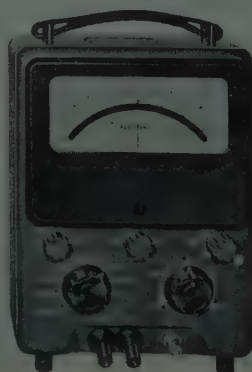
The appointment of William G. Coe (SM'56) as Pacific Division Manager of Mycalex Corporation of America has been announced. He will be responsible for sales activity in SUPRAMICA ceramoplastics and MYCALEX glass-bonded mica. He will also handle sales of telemetering switches and commutator plates for Mycalex Electronics Corporation, and represent Mycalex Tube Socket Corporation and the Synthetic Mica Company division of Mycalex Corporation of America.

A native of Illinois, Mr. Coe attended Georgia Institute of Technology in Atlanta and Rollins College, Winter Park, Fla. He held several electrical and electronics engineering positions in the eastern states before moving to California in 1951 to join the Pacific Division of Bendix Aviation Corporation, where he was a design engineer and senior engineer in telemetry. Since 1957, he has been a sales engineer for the western district office of Applied Science Corporation of Princeton.

He is a member of the Instrument Society of America and the American Radio Relay League.

For Your
DC Measurements . . .

The
Belleville-Hexem Model 110
a versatile battery-powered EIR Meter

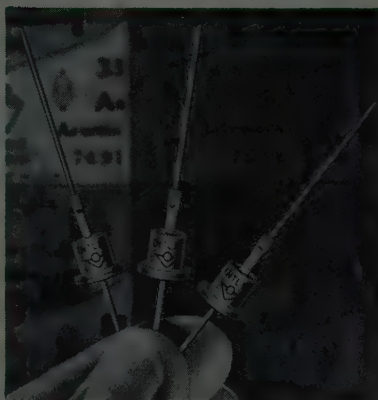


- E** • 100 millivolts to 1000 volts full scale in 9 ranges, 111 megohms input resistance
- I** • 1 millimicroampere to 300 milliampere full scale in 18 ranges, 100 millivolt voltage drop
- R** • 10 ohms to 100 megohms center scale in 6 ranges

PRICE: \$315, standard, \$350, rack

Your B-H engineering representative will be happy to arrange a demonstration. For his name and complete technical data, write The Belleville-Hexem Corporation, 638 University Avenue, Los Gatos, California.

REFLECTIVER NEWS

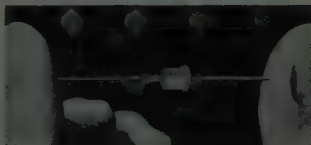


For military or industrial applications where high temperature operation is a must, International Rectifier offers two series of axial lead, hermetically sealed power diodes. Both supply full rated power under convection cooling without a heat sink.

JETEC series 1N536-1N540 and 1N1095-96 operates at -65°C to $+165^{\circ}\text{C}$ with output currents to 750ma. PIV ratings from 50 to 600v. Bulletin SR-202A describes them.

For power supply or magnetic amplifier use, 16 JETEC types are listed in Bulletin SR-132E. Ratings: 50 to 600v PIV at 300ma. Temperature range: -65°C to $+150^{\circ}\text{C}$.

The high forward conductance and extremely low leakage of these diodes permits rectification efficiencies to 99% at power frequencies; up to 70% at 50kc.



Ratings: 100 to 600 PIV, up to 500ma

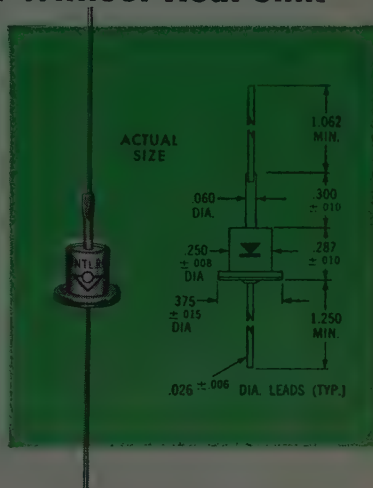
Miniaturized Silicon Diodes For Military and Commercial Use.

Write for Bulletin SR-203

Diodes in this series have been designed to provide optimum reliability and efficiency to your industrial or commercial equipment circuits. By eliminating the space consuming heat sink, you can also realize economies in equipment size as well as assembly time and costs.

Rectified dc output current ratings to 750ma at 50°C can be obtained with PIV voltages ranging from 100 to 500v.

The diode junction is hermetically sealed in an all-welded, shock-proof housing . . . a mechanical construction assuring physical strength and a positive safeguard against contaminants. This adds up to the really important feature — long term reliability! For complete specifications . . .

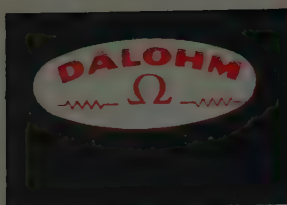


DIODE TYPES	SD-91	SD-92	SD-93	SD-94	SD-95	SD-91A	SD-92A	SD-93A	SD-94A	SD-95A
Peak Inverse Voltage, Volts	100	200	300	400	500	100	200	300	400	500
RMS Input Voltage, Volts	70	140	210	280	350	70	140	210	280	350
Continuous D.C. Voltage, Volts	100	200	300	400	500	100	200	300	400	500
Rectified D.C. Output Current, ma. at 50° C Ambient	550	550	550	550	550	750	750	750	750	750
at 100° C Ambient	300	300	300	300	300	500	500	500	500	400
Max. Surge Current (1 cycle), Amps.	10	10	10	10	10	15	15	15	15	15
Max. Operating Frequency, Kilocycles	50	50	50	50	50	50	50	50	50	50
Ambient Operating Temperature, °C	-65°C to +125°C					-65°C to +125°C				
ELECTRICAL CHARACTERISTICS										
Max. D.C. Forward Voltage Drop at 25°C	1.5 volts @ 550 ma dc (all types)					1.3 volts @ 750 ma dc (all types)				
Min. Series Resistance (Capacitive Load) (ohms)	6.8	6.8	6.8	6.8	6.8	4.7	4.7	4.7	4.7	4.7
Max. Leakage Current (mA) at Rated Continuous D.C. Voltage at 100°C	1.0	1.0	1.0	.80	.65	0.5	0.5	0.5	0.4	0.3

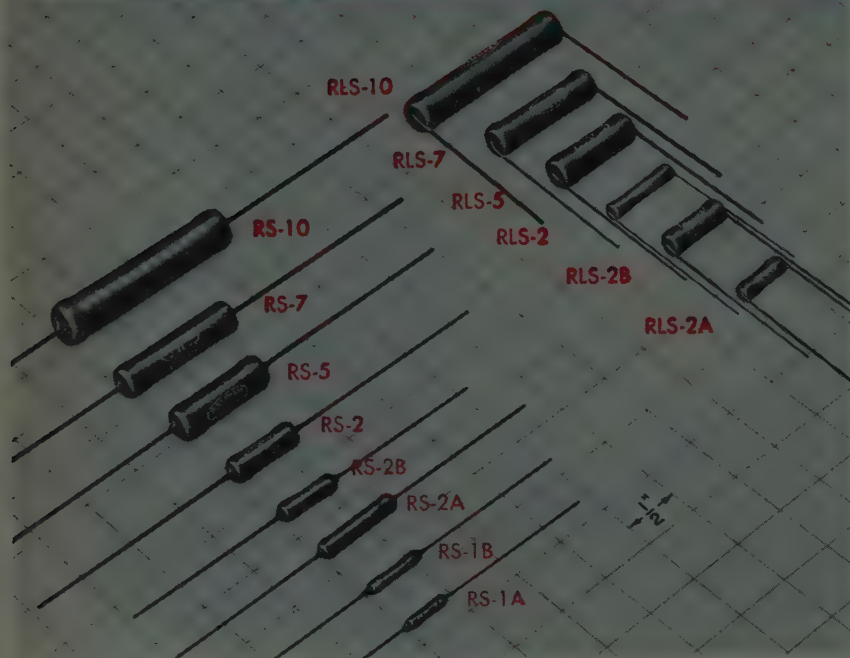
These silicon power rectifiers are designed for conduction cooling by mounting directly onto the chassis. Ratings from 400ma to one amp. are possible at PIV ratings of from 50 to 600 volts.

Power supply types 1N607 thru 1N614 and magnetic amplifier types featuring low leakage current and high forward conductance are included in Bulletin SB-135C.

JAN types 1N253, 1N254, 1N255 for the military are in full production.



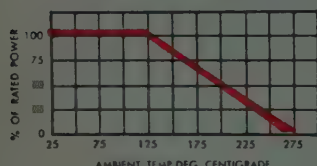
...for Complete Reliability Under
Severe Environmental Conditions



TYPE RS, RLS POWER RESISTORS

Wire Wound, Precision, Miniature, Ruggedized

RS-2A DERATING CURVE



JUST ASK US

The DALOHM line includes precision resistors (wire wound and deposited carbon); trimmer potentiometers; resistor networks; collet fitting knobs and hysteresis motors designed specifically for advanced electronic circuitry.

If none of the DALOHM standard line meets your needs, our engineering department is ready to help solve your problem in the realm of development, engineering, design and production.

Just outline your specific situation.

Designed for the specific application of high power, coupled with precision tolerance requirements. Available with axial leads—RS TYPE; with radial leads—RLS TYPE (for printed circuitry).

Gives reliability under severe environmental conditions.

- Rated at 1, 2, 3, 5, 7 and 10 watts.
- Resistance range from 0.1 ohm to 175K ohms, depending on type.
- Tolerance: $\pm 0.05\%$, $\pm 0.1\%$, $\pm 0.25\%$, $\pm 0.5\%$, $\pm 1\%$, $\pm 3\%$.

TEMPERATURE COEFFICIENT: Within 0.00002/degree C.

OPERATING TEMPERATURE RANGE: -55°C. to 275°C.

SMALLEST IN SIZE: $3/32'' \times 13/32''$ to $3/8'' \times 1-25/32''$

COMPLETE PROTECTION: Impervious to moisture and salt spray.

WELDED CONSTRUCTION: Complete welded construction from terminal to terminal.

SILICONE SEALED: Offers maximum resistance to abrasion, and has high dielectric strength.

MILITARY SPECIFICATIONS: Surpasses applicable paragraphs of MIL-R-26C.

Write for Bulletins R-23, R-30



Professional Group Meetings

ANTENNAS AND PROPAGATION

Los Angeles—September 11

"Annular Slot Direction-Finding Antenna," H. H. Hougardy, Hughes Aircraft Co.; "Periodic Slot Array Surface Wave Structure," R. W. Hougardy, Hughes Aircraft Co.

Orange Belt—September 23

"Future of Radar," W. Hausz, General Electric Co.

Washington, D. C.—June 24

"The Television Allocations Study Organization—A Progress Report," G. R. Town, Television Allocations Study Organization.

AUDIO

Boston—September 25

"Noise-Induced Mechanical Damage," Dr. J. Baruch, Bolt, Beranek and Newman, Inc.

AUTOMATIC CONTROL

Baltimore—September 16

"Trends in Automatic Control," H. Chestnut, General Electric Co., Schenectady.

Long Island—September 16

"Inertial Guidance," L. Lepschultz, Kearfott; "Sampled Data Control Systems," Dr. J. Ragazzini, New York University.

BROADCAST AND TV RECEIVERS

Los Angeles—September 18

"The Westrex Stereo-Disk System," J. G. Frayne, The Westrex Corp.

COMMUNICATION SYSTEMS

Chicago—April 11

"Microwave Terminal Section and the Carrier Terminal Equipment Used on the Miami-Havana Radio System," M. C. Gehring, A.T.&T. Co.

Florida West Coast—September 17

"Radio Frequency Interference and Associated Problems," M. Harges, Empire Devices Products Corp.

Los Angeles—June 19

"Hello, Around the World," R. Griffin, Pacific Tel and Tel Co.; "Trans-Oceanic Telephone Cable Systems," P. B. Wright, Pacific Tel & Tel Co.

ELECTRON DEVICES

Washington, D. C.—September 22

"Metal-Ceramic Construction in Electron Devices," C. P. Marsden, National Bureau of Standards.



ELECTRONIC COMPUTERS

Boston—September 15

"The Twistor—A New Solid State Memory Element," A. H. Bobeck, Bell Telephone Labs.

Philadelphia—October 2

"Recent Computer Developments in Europe," Dr. M. Rubino, Philco Corp.

San Francisco—September 16

"High Speed Logic System Using Magnetic Elements and Connecting Wire Only," H. D. Crane, Stanford Research Institute.

Washington, D. C.—October 8

"Computer Transcription of Manual Morse," C. R. Blair, Department of Defense; "Computer Ancillary for Real Time Analysis," D. L. Hogan, Department of Defense.

ENGINEERING MANAGEMENT

Chicago—May 9

"Survey of Operations Research," Dr. T. E. Caywood, Caywood Schiller Associates.

Los Angeles—September 16

"Corporate Economics and Finance," C. F. Parker, Union Oil Co.

San Francisco—October 17

"Must Engineers Be Managed More Than Most People?" G. Ewing, Lenkurt Electric Co., Inc.

INDUSTRIAL ELECTRONICS

Chicago—March 14

"Ready Reader—An Electronic Identification System for Railroad Freight cars," E. W. Ernst and R. F. Purnell, Stewart Warner Electronics.

Chicago—May 9

"Time Scale Expansion of Magnetic Records in Data Processing," M. E. Anderson and R. W. Bull, Armour Research Foundation.

INSTRUMENTATION

Chicago—November 8, 1957

"Techniques for Automatic Testing of Electronic Components," V. Walters, Cook Research.

Chicago—March 14

"Basic Electrical Instruments," H. R. Brownell, Sensitive Research Inst. Corp.

Florida West Coast—October 1

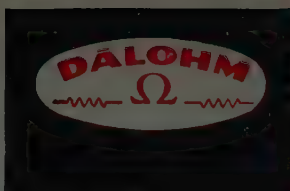
"Ultra Short Pulse Measurement," T. P. Lang, Jr., Sperry Microwave Electronics Co.

MEDICAL ELECTRONICS

Boston—October 6

"Substantial Research in Environmental Physiology," Dr. R. Goldman, U.S. Quartermaster Corp.

(Continued on page 62A)



...for Complete Reliability Under Severe Environmental Conditions



TYPE A10-W TRIMMER POTENTIOMETERS

Wire Wound, Precision, Sub-Miniature, Ruggedized

A10-W Trimmer Potentiometers are completely sealed for high temperature operation; with ruggedized construction, they provide reliability under the most severe operating conditions. Four designs available for the demanding space requirements of precision circuits.

- Rated at 1 watt up to 70° C. ambient temp.
- Resistance range from 10 ohms to 30K ohms.
- Standard tolerance: $\pm 5\%$, closer tolerance available.

RESOLUTION: .1% to 1%, depending on resistance.

OPERATING TEMPERATURE RANGE: —55° C. to 150° C.

INSULATION RESISTANCE: 1000 megohm minimum at 500 VDC at room temp.

END RESISTANCE: Not greater than 4%.

TEMPERATURE COEFFICIENT OF TRIMMER UNIT: Within ± 100 parts per million.

SUB-MINIATURE SIZE: .220 X .312 X 1.250 inches.

SCREW ADJUSTMENT: Fully adjustable throughout 25 turn range.

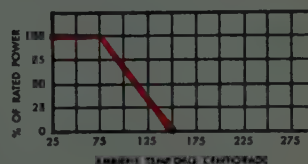
SHAFT TORQUE: 7 inch/ounce maximum.

SAFETY CLUTCH: Clutch arrangement on movable wiper contact prevents breakage due to over-exursion.

SELF-LOCKING ADJUSTMENT: Wiper will not shift under severe vibration or shock.

MILITARY SPECIFICATIONS: Surpasses applicable paragraphs of MIL-R-19A, MIL-R-12934A, MIL-E-5272A and MIL-STD-202A.

TYPICAL DERATING CURVE



JUST ASK US

The DALOHM line includes precision resistors (wire wound and deposited carbon); trimmer potentiometers; resistor networks; collet fitting knobs and hysteresis motors designed specifically for advanced electronic circuitry.

If none of the DALOHM standard line meets your needs, our engineering department is ready to help solve your problem in the realm of development, engineering, design and production.

Just outline your specific situation.

Write for Bulletin R-32

**DALE
PRODUCTS
INC.**

1302 28th AVE.
COLUMBUS, NEBRASKA

TUBE PRODUCTION IS A SCIENCE AT VARIAN

Air washed assembly

Varian Microwave tubes must be particle-free if they are to meet rigid performance standards. Varian Factory Engineers met this challenge by developing air washed production areas in which vital tube components are assembled in a continuous flow of clean filtered air.

This is typical of the attention to detail and production skill that have made Varian Tubes the **Standard** for "out-ahead" microwave equipment. Over 100 of these tubes are described and pictured in our latest catalog. Write for your copy today.

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KLYSTRONS, TRAVELING WAVE TUBES, BACKWARD WAVE OSCILLATORS, LINEAR ACCELERATORS, MICROWAVE SYSTEM COMPONENTS, R.F. SPECTROMETERS, MAGNETS, MAGNETOMETERS, STALOS, POWER AMPLIFIERS, GRAPHIC RECORDERS, RESEARCH AND DEVELOPMENT SERVICES

Professional Group Meetings

(Continued from page 61A)

Washington, D. C.—October 2

"Recent Developments in the Study of the Regulation of Blood Circulation," Dr. S. Sarnoff, National Heart Institute.

MICROWAVE THEORY AND TECHNIQUES

Long Island—September 23

"Semiconductor Microwave Switching," R. V. Garver, Diamond Ordnance Fuze Lab.

Washington—September 16

"The Effect of Neutron Bombardment upon the Microwave Properties of Certain Ferrites," N. Sakootis, Naval Research Labs.

MILITARY ELECTRONICS

Chicago—March 14

"Cooling of Electronic Equipment on Aircraft and Missiles," D. Carlson, Rotron Mfg. Co.

PRODUCTION TECHNIQUES

San Francisco—September 30

"Metal Deposition," F. J. Jensen, Varian Associates, and F. Ura, Hewlett-Packard Co.

RELIABILITY AND QUALITY CONTROL

Chicago—January 10

"Some Practical Considerations in Incoming Inspection and Quality Control of Transistors Used in Audio Applications," A. Kondrotas, Beltone Hearing Aid Co.

Chicago—September 13

"A new Approach to the Human Element in Quality Control," C. Blahna, Motorola, Inc.

Florida West Coast—September 24

"Reliability Systems Testing at Honeywell," M. Smith, Minneapolis-Honeywell Regulator Co.

Los Angeles—September 15

"Some Aspects of the Reliability Problems in Nuclear Weapons," L. A. Paddison, Sandia Corp.

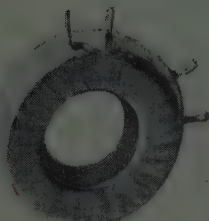
VEHICULAR COMMUNICATIONS

Florida West Coast—October 8

"Transistor Fundamentals and Applications," R. Hoffman, Electronic Communications Inc.

10 CPS SO WIDE IN RANGE... 8.0 MC

SO SMALL IN SIZE



ESC WIDE BAND VIDEO TRANSFORMERS have been engineered and developed to offer... subminiature units of unusually wide bandwidth (10 CPS to 8.0 MC). They are used to replace bulkier and more costly components, thereby creating greater economy, and increasing equipment efficiency. There are 14 catalog units available from stock, cased or uncased.

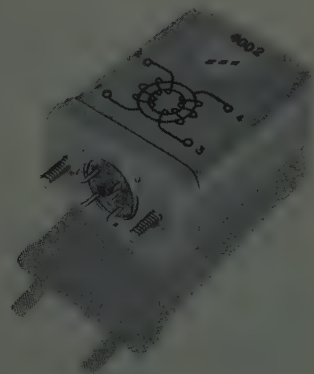
ESC ELECTRONIC COMPONENTS DIVISION specializes in

the design and development of Wide Band Video Transformers to meet your particular applications. Each transformer prototype is accompanied by a comprehensive laboratory report, which includes submitted electrical requirements, photo-oscillograms (which indicate input and output pulse shape and output rise-time), the test equipment used, and evaluation of the electrical characteristics of the prototype.

Transformers Are Supplied With Solder Terminals

Meet All Applicable Mil-Specs

Complete catalog data on request



electronic components division

ESC

CORPORATION • 534 BERGEN BOULEVARD • PALISADES PARK, NEW JERSEY

exceptional employment opportunities for engineers experienced in pulse techniques

ulse transformers • Medium and low-power transformers • Filters of all types • Pulse-forming networks • Shift registers • Miniature plug-in components • High-voltage transformers

Designed for



Application



The No. 90901

One Inch

Instrumentation Oscilloscope

Miniaturized, packaged panel mounting cathode ray oscilloscope designed for use in instrumentation in place of the conventional "pointer type" moving coil meters uses the 1" 1CP1 tube. Panel bezel matches in size and type the standard 2" square meters. Magnitude, phase displacement, wave shape, etc. are constantly visible on scope screen.

**JAMES MILLEN
MFG. CO., INC.**

**MAIN OFFICE AND FACTORY
MALDEN
MASSACHUSETTS**



Industrial Engineering Notes*



EIA ACTIVITIES

A new directory listing electronics manufacturers in the Los Angeles area has been printed and is available from the Industrial Department, Los Angeles Chamber of Commerce, at \$2.50 per volume. The directory not only lists the firms but such details as plant size, amount of personnel, type of business, products, and market areas served. Military purchasing and liaison officers in the Los Angeles area are also listed.

MILITARY ELECTRONICS

The nation's new civilian space agency, the National Aeronautics and Space Administration, began operating recently and with added funds totaling \$218.1 million. This brings the total NASA monies to \$298.1 million for fiscal year 1959. In addition to the \$80 million appropriated by Congress for the first year's operation of NASA, the agency inherited \$59.2 million in transfer funds from the Advanced Research Projects Agency, \$57.8 million from the Air Force to cover planned NASA work on engines, and \$101.1 million for continuing the functions of the National Advisory Committee for Aeronautics (NACA). At the same time, the new space agency was given jurisdiction over the "United States scientific satellite project VANGUARD," and specific projects of the ARPA and the Air Force which relate to space activities "including lunar probes, scientific satellites and super-thrust boosters" within the scope of the functions as provided by the Space Act of 1958. . . . A new "three-dimensional" radar which detects airborne targets at extreme range and for the first time simultaneously computes distance, bearing and altitude, was unveiled last week by the Department of the Army. Called FRESCANAR, the new radar was developed by the Hughes Aircraft Co. It is considered to be the eyes of "missile monitor," an Army air defense guided missile fire distribution system for mobile use with a field army and is ready for operational use with air defense missile batteries. . . . The Air Research and Development Command announced development of a "dynamic analyzer" to test reliability of reconnaissance equipment on space vehicles. The equipment simulates most known conditions of outer space and can be modified to include other conditions as they become known, ARDC said. Heretofore, aerial reconnaissance equipment has been static-tested in the laboratory, then flight-tested in an aircraft. The new system is expected to provide a more accurate analysis of systems before they reach flight test stage.

PRODUCTION AND PERSONNEL

Demand for engineers rose materially during the summer, partly as a result of expanding missile production, the Labor Department reported. Since July, shortages of engineers have showed up in 45 states; the Department's Bureau of Employment Security said. The number of unfilled engineering job openings for which qualified applicants were not available locally totaled 4,335 late in September, an increase of 1,400 over July and up 400 from September a year ago, the Labor Department said. A nationwide professional placement network of 83 key local employment offices reported in September a total of 8,534 professional and managerial job openings for which it was recruiting applicants. Slightly more than half of these openings were for engineers, and the greatest demand was for electrical and mechanical engineers, specialties needed by manufacturers of missiles, it was said. . . . TV production in August totaled 507,526 compared with 274,999 TVs made in July and 673,734 television receivers produced in August 1957. Cumulative TV output during the January-August period of this year amounted to 2,930,455 compared with 3,756,533 TV receivers made in the same period last year. Radio receiver production in August totaled 1,018,832 including 242,915 automobile radios compared with 621,541 radios made in July, which included 186,379 auto sets, and 965,724 radios made in August 1957 which included 301,971 auto sets. Cumulative radio receiver production during the first eight months of this year totaled 6,611,686 including 1,893,813 automobile receivers compared with 8,765,606 radios made during the like eight-months period last year, which included 3,392,926 auto sets. . . . Applied Research and Development expenditures by American industry for Electronics amounted to \$1.4 billion during the year 1956. This estimate is being released by the Electronic Industries Association through the courtesy of the National Science Foundation. Compiled by the U. S. Bureau of Labor Statistics on the Foundation's behalf, it is the first comprehensive survey ever conducted which reveals the major industrial research and development effort being made in the Electronics field. Ninety-eight per cent of the \$1.4 billion applied electronic research and development work was performed by fifteen industries as shown below in Table I.

(Continued on page 68A)

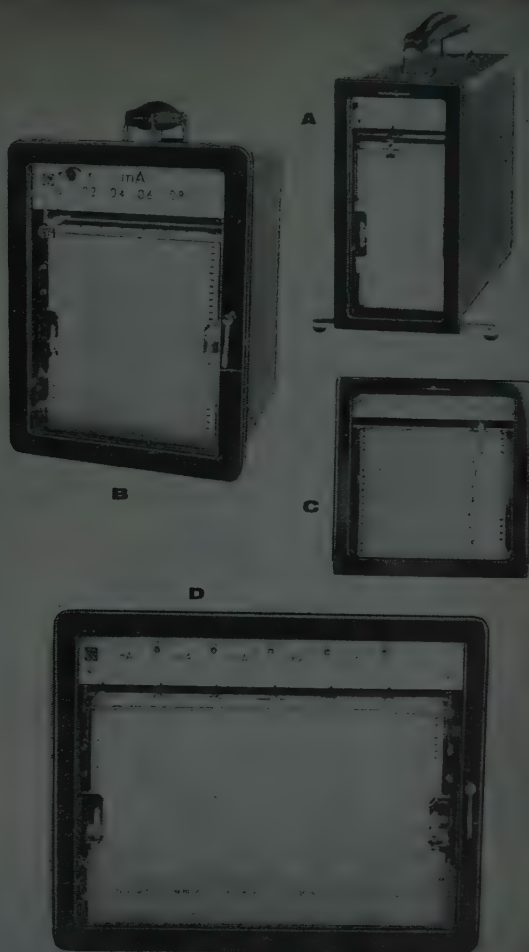
* The data on which these NOTES are based were selected by permission from *Industry Reports*, issues of September 29, and October 6, 13, and 20, published by the Electronic Industries Association whose helpfulness is gratefully acknowledged.



Curtiss-Wright RECTILINEAR STRIP CHART RECORDERS

offer you

12 BIG ADVANTAGES



1 MOVING-COIL AND DYNAMOMETER MOVEMENTS

— No choppers, tubes, motors, slidewires, mirrors . . . provides utmost reliability. AC, DC, and Power movements.

2 UP TO 6 CHANNELS AVAILABLE

— Curtiss-Wright Double Size Models are the only Rectilinear Strip Chart Recorders to offer up to 6 channels. Curtiss-Wright recorders provide simultaneous recording of two to six variables on a single chart in any combination of different types of movements.

3 SENSITIVITY DOWN TO 250 μ A FOR DC

. . . can be extended beyond 250 μ A by DC amplifier (optional).

4 ACCURACY 1% FOR MOVING-COIL RECORDERS

— Conservatively rated as $\pm 1\%$ of full scale for DC movements. Unusually low friction of pen against chart.

5 INKLESS AND INK RECORDING

— Inkless recording is standard equipment on all but Miniature Models, on which it is optional. Cleanest, easiest method . . . a fine metal stylus "burns" the record into zinc coated chart paper. Instantly converted to ink recording.

6 RECTILINEAR RECORDING

— A patented mechanical linkage changes angular motion of the needle into a straight line, giving an undistorted picture of the signal. Avoids errors and saves time.

7 THREE-SPEED TRANSMISSION

plus 60:1 speed change from hours to minutes provides six interchangeable speeds in all.

8 MOTOR AND SPRING DRIVES

— Sync motor, hand-wound short drive or electrically wound spring motors. Automatic chart rewind.

9 LIGHT AND COMPACT DESIGN

— Small size and advanced design engineering of movement allows space and weight savings.

10 DUST-PROOF AND SPLASH-PROOF CASES

— Steel cases decrease effect of stray magnetic fields.

11 SHOCK-PROOF MOVEMENT

— Extra reliability when used in portable applications.

12 OUTSTANDING WORKMANSHIP

— Improved design and meticulous attention to detail assure highest quality precision performance. All Curtiss-Wright recorders carry a one-year guarantee.

Curtiss-Wright . . . a new name in rectilinear strip chart recorders . . . offers you time proven advantages in precision operation. Made under licensing agreements with Metrawatt AG . . . a leading West German manufacturer of fine instruments for over 50 years . . . Curtiss-Wright recorders combine advanced design with highest quality workmanship. Moderate in price, these fine precision instruments are rugged and reliable . . . simple to operate. Write for complete information.

ELECTRONICS DIVISION

CURTISS-WRIGHT

CORPORATION • CARLSTADT, N.J.

ILLUSTRATED ABOVE

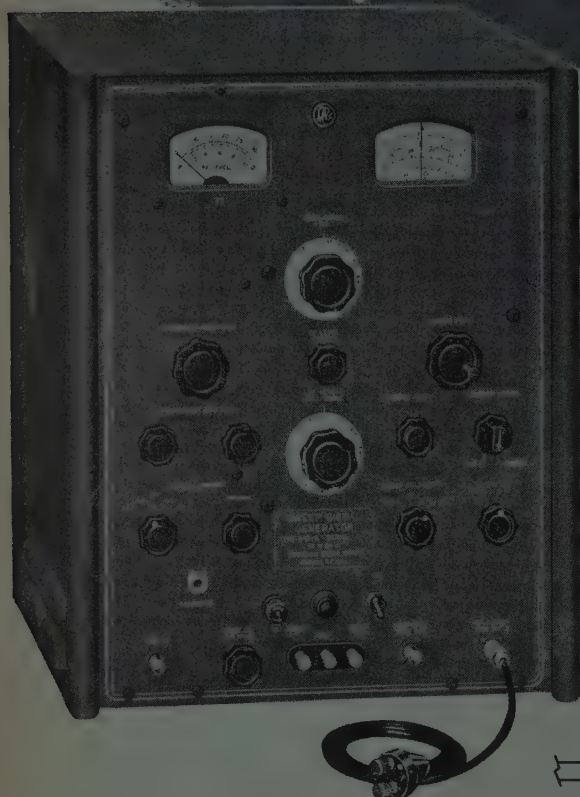
A — MINIATURE SLIM MODELS 86 (portable) and 87 (flush). Weigh 9 lbs. $3\frac{3}{4}$ " x $7\frac{1}{4}$ " x $8\frac{3}{4}$ ". \$295.00 and up

B — STANDARD MODELS 81 (portable) and 82 (flush). Weigh 19 lbs. $7\frac{1}{2}$ " x $9\frac{1}{8}$ " x $8\frac{1}{2}$ ". \$445.00

C — MINIATURE SQUARE MODEL (85) Weighs 16 lbs. $5\frac{3}{8}$ " square, $12\frac{1}{4}$ " deep. \$330.00 and up

D — DOUBLE SIZE MODEL 83 (portable) and 84 (flush). Weigh 26 lbs. $12\frac{3}{4}$ " x $9\text{--}13\frac{1}{16}$ " x $8\frac{3}{4}$ ". \$860.00 and up

Sweep Frequency Coverage

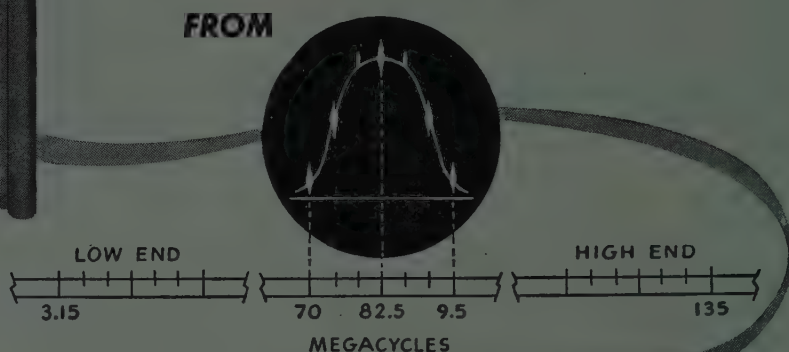


with this

BRC SWEEP SIGNAL GENERATOR

Type 240-A

having Crystal-Referenced Birdie-Type Markers and two individually controlled Pip Interpolation Markers



USE THIS SWEEP GENERATOR FOR

- (1) The determination of selectivity and sensitivity of test circuits,
- (2) The study of band-pass characteristics,
- (3) The adjustment of stagger tuned circuits,
- (4) The determination of linearity of FM discriminators, and
- (5) The study of crystal modes.

Features include (A) Crystal-Referenced Birdie-Type Markers, (B) Adjustable Pip-Interpolation Markers, and (C) A composite signal containing the markers added to the response of the system under test. Provisions have also been made for operation as a C.W. or A.M. Signal Generator.

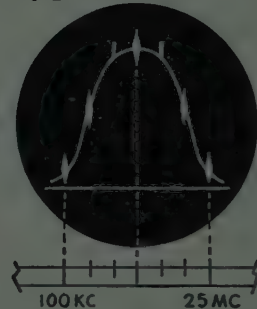
CENTER FREQUENCY: 4.5 MC to 120 MC, accurate to $\pm 1\%$, continuously variable in five self-contained ranges. Output frequencies are fundamental oscillations.

SWEEP WIDTHS: Continuously variable from $\pm 1\%$ to $\pm 30\%$ of center frequency or ± 15 MC, whichever is smaller.

PRICE: \$1585.00 F.O.B. Boonton, New Jersey



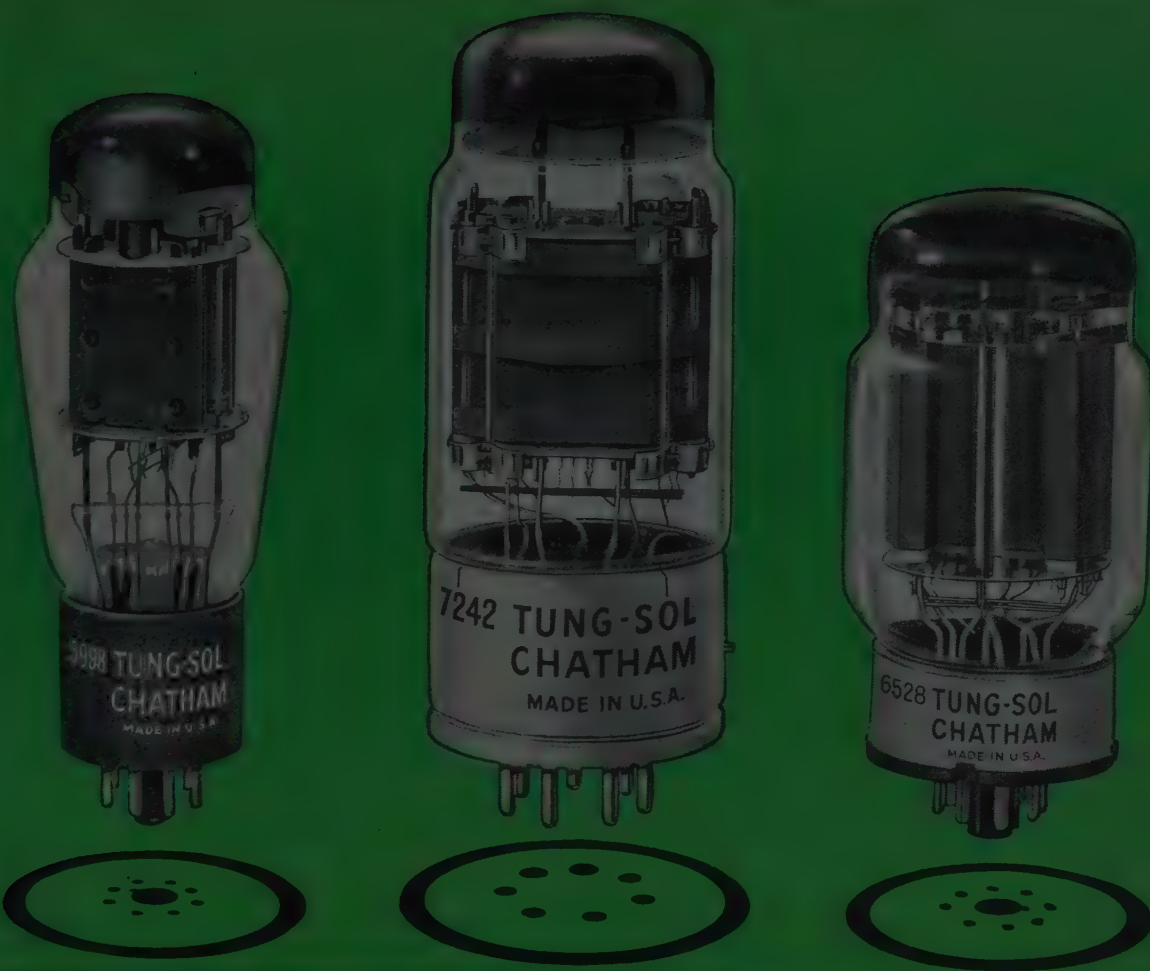
TO



TYPE 203-B UNIVERTER

This accessory, a frequency converter having unity gain, effectively extends the low-frequency range of the Type 240-A Sweep Signal Generator down to approximately 100KC.

PRICE: \$380.00 F.O.B. Boonton, New Jersey



Tung-Sol/Chatham power triode family covers every series regulator need!

Now designers can specify a premium quality Tung-Sol/Chatham tube for all series regulator sockets. Tung-Sol/Chatham's family of power triodes—the first designed and produced specially for series regulator service—meets all design requirements and assures maximum reliability and life at all times.

Types include the new 100 Watters, 7241 and 7242, medium mu or low mu-high current, 12 or 26 Volt

heater versions available on most types. All embody sturdy construction features that contribute to overall ruggedness and long hours of heavy-duty operation.

Compare the ratings below against your particular application! If you desire complete data sheets . . . or you have a specific design problem, contact us today! We'll be glad to give whatever assistance we can. Just write: Tung-Sol Electric Inc., Newark 4, N. J., Commercial Engineering Offices: Bloomfield and Livingston, N. J., Culver City, Calif., Melrose Park, Ill.

TYPICAL VALUES

	Total Plate Current	Range of Tube Voltage Drop	Minimum Tube Drop	Grid Voltage Swing
5998	200 ma	80 v	45 v	20 v
6528	400	65	70	10
7242	600	80	70	13

PERTINENT CHARACTERISTICS PER TUBE

	Max. Plate Current	Max. Plate Voltage	MU	Gm
5998	280	275	5.5	28,000 umhos
6528	600	400	9.0	74,000 umhos
7242	900	400	9.0	111,000 umhos

ts TUNG-SOL®

TUBE TYPES BY PLATE DISSIPATION RATINGS

Total Plate Dissipation	26 to 30 W	60 W	100 W
Low Mu	6AS7G, 6082	6336A	7241
	6080WA, 7105	6394A	
Medium Mu	50L3	6528	7242

BEEDE

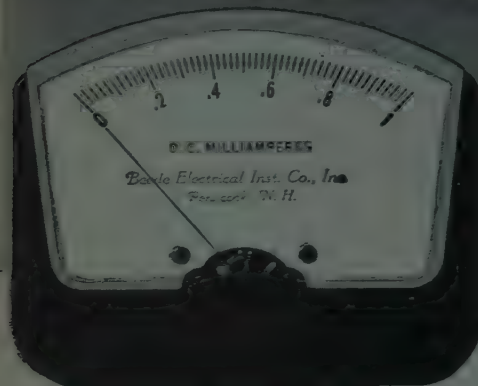
INDICATING INSTRUMENTS

the PANORAMA

AVAILABLE IN

3

SIZES



Model 70	Model 230	Model 140
Width 7"	Width 4 1/2"	Width 3 1/2"
Height 5 1/4"	Height 3 1/2"	Height 2 5/8"

The PANORAMA gives you better, clearer vision longer scales, easier readability. The plastic panel provides excellent natural illumination; top, sides and front.

Available with frosted portion or color of your choice.

The ultra modern beauty of the PANORAMA will add much to your product.

Send for Complete Information

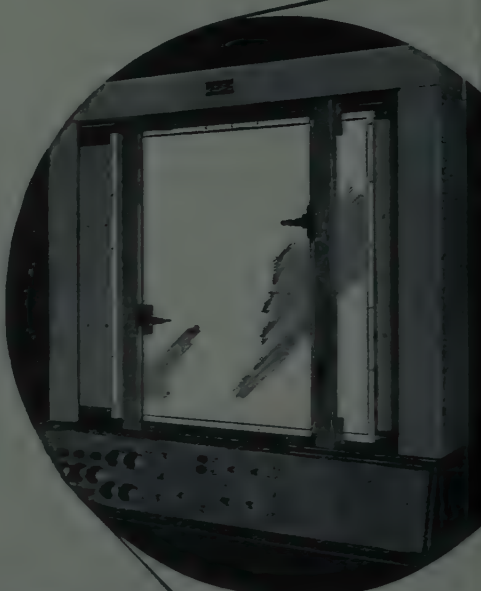
BEEDE ELECTRICAL INSTRUMENT CO., INC.
PENACOOK, NEW HAMPSHIRE

ELECTRONIC
ASSOCIATES
Incorporated

LONG BRANCH, NEW JERSEY • CAPITOL B-1100

- Smaller Size
- Less Weight
- Faster Response
- Greater Reliability
- Instant Warm-up

EAF's new Transmired Variplotter, Model 205-T, assumes these X-Y plotting advantages and includes many more — vertical or horizontal operation, disposable ink cartridges, vacuum hold-downs, established reputation, etc. Bulletin No. PDR-441 further details these advantages.



EAF's new Transmired Variplotter.

Have you explored the advantages of analog simulation in solving your design problems? Write for Application Bulletin describing successful applications in your industry.

Industrial Engineering Notes

(Continued from page 64A)

Industry	Value of Applied R & D Expenditures For Electronics (in millions of dollars)
Electronic-Electrical Systems, Parts Aircraft and Associated Parts	\$ 669.6
Machinery (including computers)	260.7
Telecommunications and Broad- casting	182.1
Professional and Scientific Instru- ments	137.0
Fabricated Metal Products and Ord- nance	64.5
Stone, Clay and Glass Products	36.7
Food and Kindred Products	4.4
Textile Mill Products and Apparel	4.0
Petroleum Products and Extraction	1.1
Primary Metals	0.8
Chemicals and Allied Products	0.8
Transportation and Other Public Utilities	0.4
Construction	0.3
Paper and Allied Products	0.1
All Other Industries	0.1
Total	30.3
	\$1,392.9

These industries are grouped in accordance with the Standard Industrial Classification and therefore include both manufacturing and certain non-manufacturing industries. Other sectors of the economy such as government, universities, commercial laboratories and non-profit institutions are excluded. Research and development expenditures for the "sciences (including medicine); engineering, design and development of prototypes and processes" are counted. However, the Foundation's study omitted cost of "quality control, routine product testing, market research, sales promotion, sales service, research in the social sciences and psychology, and other non-technological activities and technical services." It should be noted that the electronic expenditure represents *applied* research and development only to the exclusion of *basic* research. The National Science Foundation defines applied research as including projects "directed to discovery of new scientific knowledge which have specific commercial objectives. . . ." By contrast, basic research includes projects "which represent original investigation for the advancement of scientific knowledge and which do not have specific commercial objectives, but may occur in fields of present or potential use. . . ." Development is defined as "technical activity concerned with non-routine problems which are encountered in translating research findings or other general scientific knowledge into products or processes. It does not include routine technical services to customers" or the items mentioned above. Electronics in applied research and development pertains to electronic systems and components, whether for wire and wireless telephone and telegraph of all kinds, radio and television transmitting and receiving, object detection, industrial controls, business machines, or other applications." The total cost of R & D expenditures, both applied and basic, incurred by industry for all purposes including electronics amounted to \$6.5 billion during 1956 according to the preliminary report issued by the National Science Foundation. This total is up 76% over the \$3.7 billion cost during 1953.

MICROWAVE GENERATORS

950 to 21,000 mc

with MORE MODULATION CAPABILITIES

The extremely wide range of pulse width, delay and repetition rate are read directly on the front panel of Polarad microwave generators. In addition these units provide broadband internal FM and CW modulation, versatile external modulation capability and a sync output for all signals. These features provide the largest choice of microwave test signal combinations available in signal generators.

Internal pulse rise and decay: 0.1 microsecond.*

External pulse modulation: positive or negative polarity, 10 to 10,000 pps, 0.2 to 100 microseconds width.*

Output synchronization pulses: positive polarity, delayed and undelayed.

Rugged construction. Quick, easy inspection and servicing. Continuous UNI-DIAL tuning in each frequency range. Non-contacting tuning cavity chokes.

For every application, 950 to 21,000 mc.

Model	Frequency Range	Power Output
MSG-1	950 to 2,400 mc	0 dbm (1 milliwatt) to -127 dbm, directly calibrated
MSG-2	2,000 to 4,600 mc	
PMX	4,200 to 8,000 mc	
MSG-34	6,950 to 11,000 mc	
PMK	4,200 to 11,000 mc	+10 dbm (10 milliwatts) to -90 dbm
	10,000 to 15,500 mc	
	15,000 to 21,000 mc	

AND MICROWAVE POWER SOURCES — 1,050 to 17,500 mc.

High power output: 14 to 700 milliwatts depending on frequency. Modulation: Internal square wave or external FM and square wave.



POLARAD ELECTRONICS CORPORATION

43-20 34th Street

Long Island City 1, N. Y.

Representatives in principal cities

MAIL THIS CARD for specifications. Ask your nearest Polarad representative (in the Yellow Pages) for a copy of "Notes on Microwave Measurements."

MODULATION CAPABILITIES*

Generates CW, FM, internal pulse, internal square wave. Or can be externally modulated.

Pulse delay: adjustable from 2 to 2,000 microseconds.

Pulse repetition rate: adjustable from 10 to 10,000 pps.

Pulse width: adjustable from 0.2 to 10 microseconds.

Linear sawtooth internal FM modulation, 10 to 10,000 cps, 5 mc minimum frequency deviation.

Internal or external, pulse or sine wave synchronization.

*Models MSG-34, PMX and PMK

POLARAD ELECTRONICS CORPORATION:

Please send me complete specifications for:

☐ Microwave Signal Generators,

to _____

☐ Microwave Power Sources,

to _____

My application is: _____

Name _____

Title _____

Dept. _____

Company _____

Address _____



MICROWAVE GENERATORS

18,000 to 50,000 mc.

MICROWAVE SIGNAL GENERATORS

18,000 to 39,000 mc

7 interchangeable plug-in tuning units
Calibrated power output: -10 to -90 dbm
Direct-reading attenuator, accurate to 2%

MICROWAVE POWER SOURCES

18,000 to 50,000 mc

9 interchangeable plug-in tuning units
High power output: 10 mw from
18,000 to 33,520 mc.
Between 9 and 3 mw in higher ranges,
depending on frequency.

PLUG-IN INTERCHANGEABILITY

Now you can work at Extremely High Frequencies with one basic microwave generator, using only the tuning units in the ranges you require immediately. Later, as your work expands to other frequencies, add only tuning units — not complete generators.

All instruments provide: a direct reading wavemeter, indicating frequency to 0.1% accuracy; continuous tuning over entire range; 1,000 cps internal square-wave modulation — or external modulation; direct waveguide output connectors. All are designed for quick, easy inspection and servicing.

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43-20 34th St., Long Island City 1, N. Y.

MAIL THIS CARD
for specifications. Ask
your nearest Polarad
representative (in the
Yellow Pages) for a copy
of "Notes on Microwave
Measurements".

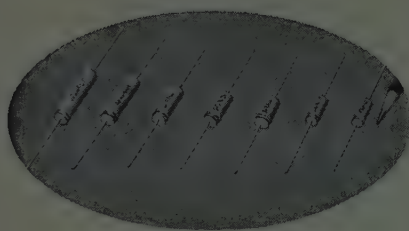
FREE LIFETIME SERVICE
ON ALL POLARAD
INSTRUMENTS

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Representatives in principal cities

TAKE YOUR PICK FROM . . . THE SPRAGUE TRANSI-LYTIC* FAMILY

of **tiny** electrolytic capacitors
for every requirement in entertainment electronics . . .
pocket radios, wireless microphones, miniature tape
recorders, auto receivers



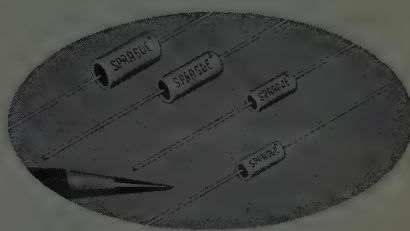
LITTL-LYTIC* CAPACITORS

Sprague's new Type 30D hermetically-sealed aluminum-encased capacitors are the *tinest* electrolytic capacitors made to date . . . and their performance is better than ever. Their remarkable reliability is the result of a new manufacturing technique in which *all the terminal connections are welded. No pressure joints . . . no "open circuits" with the passage of time.* And check this for ultra-low leakage current: for a 2 μ f, 6 volt capacitor . . . only 1.0 μ a max.; for a 300 μ f, 6 volt capacitor . . . 3.5 μ a max.! Engineering Bulletin No. 3110 gives the complete story. 85°C standard.



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These space-saving Type 89D 'lytics are designed for easy manual upright mounting on printed wiring boards. Keyed terminals assure fast mounting and correct polarity. No reworking on the assembly line. Sturdy pre-molded phenolic shell with resin end-fill gives excellent protection against drying-out of the electrolyte or the entry of external moisture. The phenolic case eliminates the necessity for additional insulation. Reasonably priced for mass production receivers. Engineering Bulletin No. 3060 lists standard ratings with performance data.



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*Trademark

FOR ENGINEERING BULLETINS on the industry's first complete line of subminiature aluminum electrolytic capacitors, write Technical Literature Section, Sprague Electric Company, 230 Marshall Street, North Adams, Massachusetts.



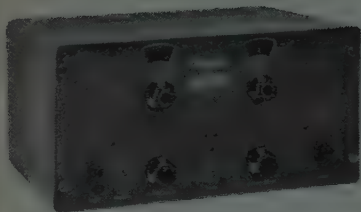
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340-A	Servo	.01 cps to 100 cps	\$385.00
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(Continued on page 72A)

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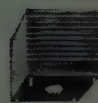
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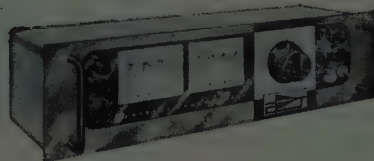
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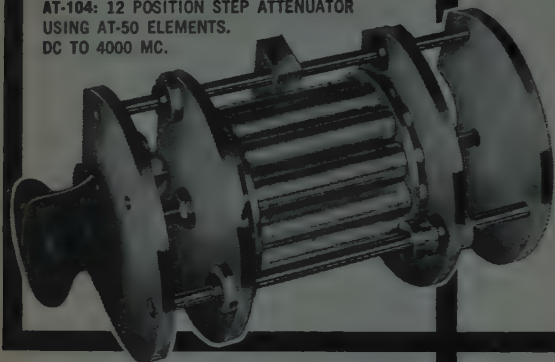
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AT-104: 12 POSITION STEP ATTENUATOR
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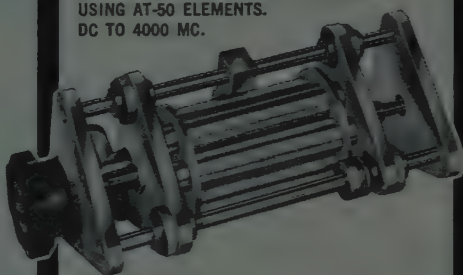
Empire's UHF attenuators are resistive coaxial networks for the frequency range from DC to 4000 MC.

Accuracy is held to $\pm 1/2$ DB, VSWR is better than 1.2 to 1. Any attenuation values up to 60 DB (120 DB for Model AT-106), are available. Deposited carbon elements are used for stability and operations at higher pulse levels. Standard impedance is 50 ohms, other values upon request. These units have excellent temperature characteristics and are vibration and shock resistant. Standard connectors are type "N", attenuator pads are also available with type "C".

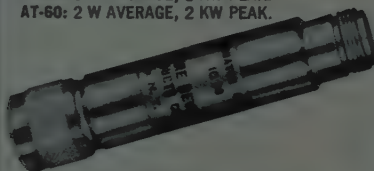
The attenuators may be obtained as individual pads (AT-50, AT-60), or as multi-position step attenuators AT-103 (six positions) and AT-104 (twelve positions). For even greater flexibility, Attenuator Panels, Model AT-106 (two or three step attenuators in series connected) are recommended.

For complete technical information
about attenuators for your
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AT-103: 6 POSITION STEP ATTENUATOR
USING AT-50 ELEMENTS.
DC TO 4000 MC.



ATTENUATOR PADS.
DC TO 4000 MC.
AT-50: 1 W AVERAGE, 1 KW PEAK.
AT-60: 2 W AVERAGE, 2 KW PEAK.



AT-106: ATTENUATOR PANEL.
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(Continued on page 74A)



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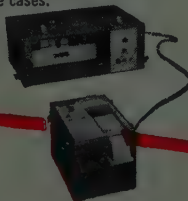


MODEL 276 CHART VIEWER

Permits convenient, variable speed editing and study of Sanborn charts and other types up to 16" wide, 200 ft. long. Single control for direction, paper speeds (15" to 100"/min). Transparent cursor slides left or right, adjusts for accurate alignment with coordinates.

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Features of the "150 series" direct writers include: frequency response to 100 cps; linearity 1% overall; inkless recording in true rectangular coordinates by heated stylus on plastic coated Permapaper charts; current feedback driver amplifier and regulated power supply for each channel. Recorder has 9 chart speeds, 0.25 to 100 mm/sec; individual stylus heat controls, time-code marker. Up to 6-channels can be housed in one vertical cabinet. Amplifiers, recorder also available in individual portable cases.



6-, 8-CHANNELS, FLUSH FRONT RECORDER, FREQUENCY RESPONSE TO 120 CPS 350 SERIES

New "350" series direct writers with compact plug-in preamps in modules of up to 4; individual power supplies; current feedback transistorized power amplifiers; limiter circuit ahead of power amplifiers; velocity feedback galvanometer damping; enclosed galvanometers. Linearity 0.2 div. over entire 50 divisions. Recorder-power amplifier-power supply package has 0.1 volt/div. sensitivity, can be used separately; pushbutton controls for 9 chart speeds 0.25 to 100 mm/sec; individual stylus heat controls; contacts for remote control; inkless rectangular coordinate recording on Permapaper charts.



6-, 8-CHANNELS 850 SERIES

Compact "850" series direct writers use 7" high plug-in preamplifiers in modules of up to eight and "350" flush front recorder package with transistorized power amplifiers, power supply; features velocity feedback galvanometer damping; linearity 0.2 div. over entire 50 divisions; 9 chart speeds from 0.25 to 100 mm/sec controlled by electric push-buttons; inkless recordings on Permapaper charts. Available preamps include Servo Monitor (demodulator) and DC Coupling. Carrier, Chopper Stabilized and Low Level types are in development.

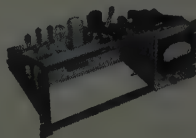


COMPUTER READOUT WITH AUTOMATIC PROGRAMMING 150 SERIES

"150 series" 6-, 8-channel consoles in 46 1/2" high mobile cabinet. Dual-Channel Amplifiers have selectable sensitivity from 0.01 to 10 volts/div.; internal calibration 2 volts \pm 1% freq. response flat to 20 cps. Optional Programmer sequences system operation in 20 steps, including recorder turn-on, calibration, computer DC level reading, recording for pre-set time, turn-off and reset.



PORTABLE INDICATORS FOR STRAIN, ETC.



Model 150-300/700 Wide Band Amplifier and Power Supply accepts "150" series preamplifiers — for use with low power galvanometers, oscilloscopes, panel meter. Freq. range DC to 10,000 cps (but limited by particular preamp range). Panel meter has center zero scale, 25 divisions each side of center.

SELF-CONTAINED UNIT PREAMPLIFIERS TO DRIVE 'SCOPES, OPTICAL OSCILLOGRAPHS, TAPE RECORDERS, ETC.

Portable "350" series include Carrier, DC Coupling Servo Monitor (demodulator), True Differential DC types; others in development. Mount in portable "450" cases or in four-unit modules in 19" frame. Use individual power supplies. One "450" case and power supply can serve any "350" Preamp.



(ALL DATA SUBJECT TO CHANGE WITHOUT NOTICE)

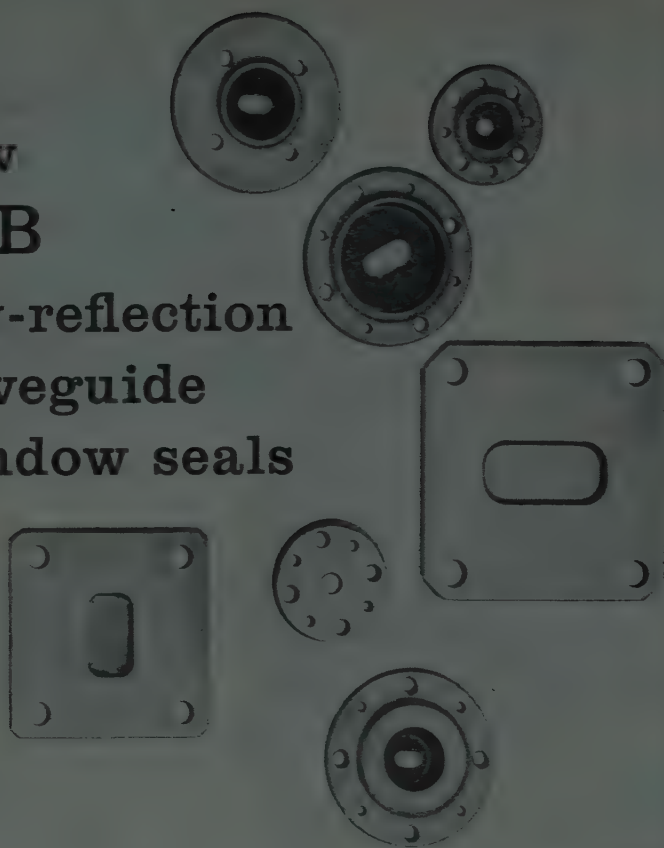
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Thermally stable. D-B seals will not fracture in desert or arctic climates ... will withstand degassing by baking. Units are vacuum-tight ... shock and vibration proof. Seven standard sizes cover the entire microwave and ultra-microwave range.

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VSWR: Averages 1.19 over entire range.

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Jackson, W. E., Salem, Mass.
Jablonski, F. J., Lutherville, Md.
Johnson, J. H., Los Angeles, Calif.
Kasani, A. A., Rawalpindi, West Pakistan
Kathley, L. W., Worcester, Mass.
Kemp, G. L., Morris Plains, N. J.
Kiser, E. R., Lees, Mass.
Kluger, I. A., Kfar Aza, Haifa, Israel
Koenig, S. E., Brooklyn, N. Y.
Kozak, M. J., Philadelphia, Pa.
Kusman, T., Madras, India
Kuntz, S. R., Brooklyn, N. Y.
Lanfear, B. B., Alhambra, N. M.
Lang, P. A., Los Angeles, Calif.
Lanfear, S. T., Sr., Fort Worth, Tex.
Lee, R. E., Los Angeles, Calif.
Lehrer, N. H., Los Angeles, Calif.
Lensi, E., Roma, Italia
Levenque, P. J., William, Mass.
Lewis, H. G., Midway City, Okla.
Looman, J. R., Santa Barbara, Calif.
Lymari, J., Los Angeles, Calif.
Mann, J. R., Brooklyn, N. Y.
Mannese, N., Bellingham, N. J.
Mannes, G. E., Hawthorne, Calif.
Martin, D. R., Granada Hills, Calif.
Mason, L. J., Ottawa, Ont., Canada
Massey, E. H., Burlington, N. C.
May, G. L., Silver Spring, Md.
McAllister, H. M., Haddonfield, N. J.
McConnell, R. A., Palo Alto, Calif.

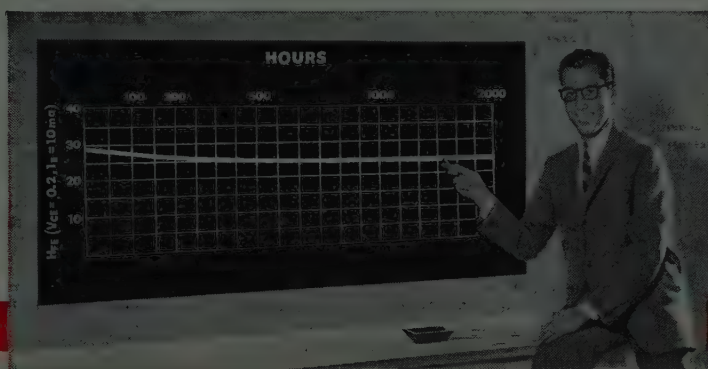
(Continued on page 76A)

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2N426
2N427
2N428

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2N404	-25	-12	-24	4.0	50	120
2N425	-30	-20	-20	2.5	30	150
2N426	-30	-20	-18	3.0	40	150
2N427	-30	-20	-15	5.0	55	150
2N428	-30	-20	-12	10.0	80	150
Temperature range -65°C to +85°C						



SYLVANIA

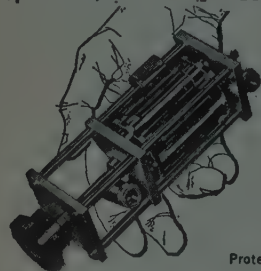
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Membership

(Continued from page 74A)

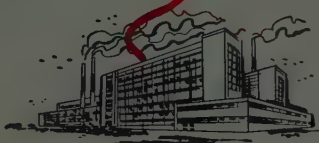
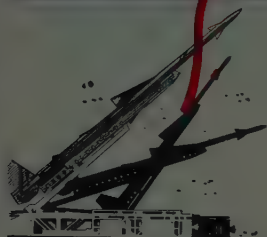
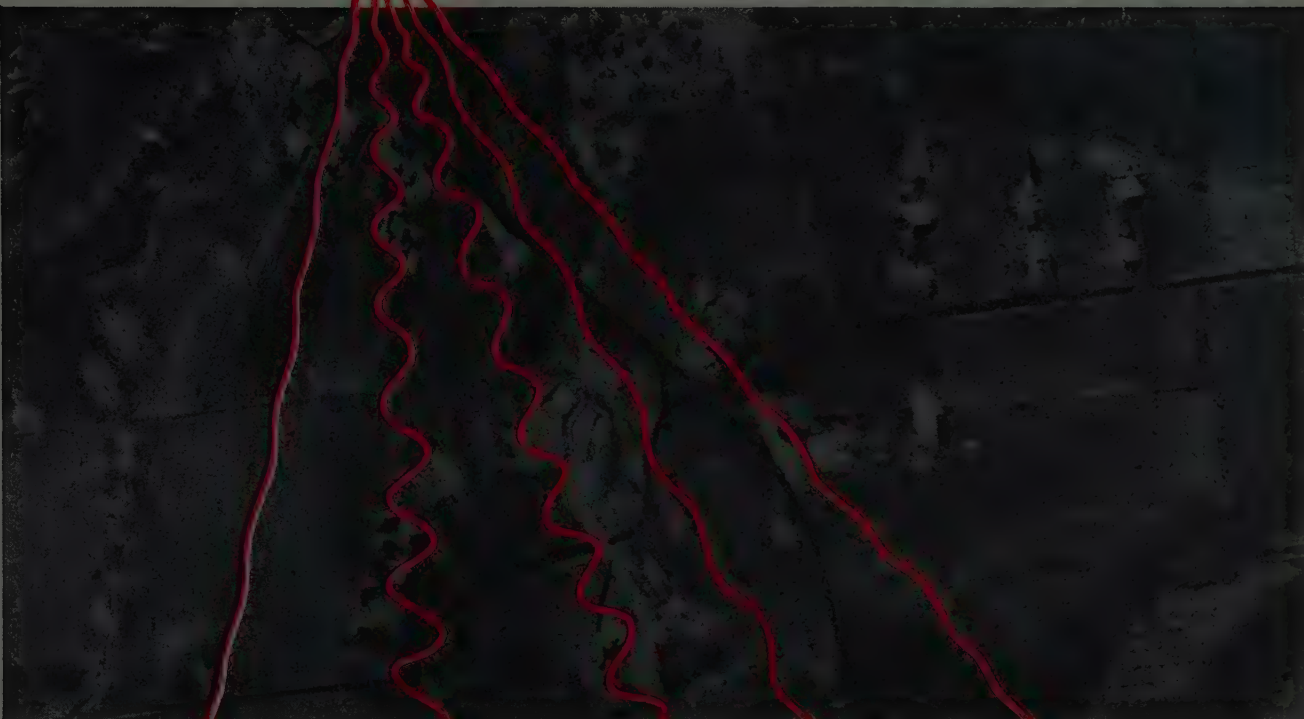
McCrary, G. W., Jr., San Diego, Calif.
McKelvey, E. J., Dearborn, Michigan
McMahon, V. J., Edmonton, Canada
McManus, R. O., Woburn, Mass.
McMullen, P. L., Burbank, Calif.
Menta, B. B., Addis Abeba, Ethiopia, Africa
Miller, D., Venice, Calif.
Mock, R. E., Holloman AFB, N. M.
Moore, J. D., San Antonio, Tex.
Moran, J. F., Jr., Kettering, Ohio
Munson, V. E., Denville, N. J.
Nachbar, M. S., Spotswood, N. J.
Nelson, J. N., Harrison, N. J.
Nenortas, K., Dorchester, Mass.
Nine, J. A., Burlington, N. C.
Nizan, A., Haifa Bat-Galim, Israel
Offner, M. M. Y., Boston, Mass.
Otsuki, Y., Akasaka Minato-ku, Tokyo, Japan
Paasch, R. H., Furlong, Pa.
Painter, R. R., Somerville, N. J.
Paris, A. P., Quebec, Canada
Parker, F. D., Irving, Tex.
Paul, A. N., Rochester, N. Y.
Pessin, L., Haddonfield, N. J.
Petitt, J. G., Cedar Rapids, Iowa
Petrilla, A. D., Philadelphia, Pa.
Pickering, R. L., Concord, Mass.
Possner, L., Culver City, Calif.
Preece, K. E., Devon, England
Price, J. M., Columbus, Ohio
Purser, C. W., Fayetteville, N. Y.
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Sackett, L. C., Los Angeles, Calif.
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Saiers, J. L., Granada Hills, Calif.
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Schneider, G., Stamford, Conn.
Schultz, H. R., Los Angeles, Calif.
Scott, R. E., Lincoln Park, Mich.
Sellers, J. D., Melbourne, Fla.
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Simpson, P. D., Rome, N. Y.
Sinkler, C. I., Sacramento, Calif.
Sinn, R. S., Seaside Park, N. J.
Skinner, K. R., Metuchen, N. J.
Slavin, H., Philadelphia, Pa.
Slocum, L. V., Bethlehem, Pa.
Smith, C. R., East Meadow, L. I., N. Y.
Smith, G. H., Littleton, Colo.
Smith, R. A., Haddonfield, N. J.
Sowell, P. W., Castellana, Madrid, Spain
Speers, D. F., Natick, Mass.
Spray, W. D., Glendale, Calif.
Stephenson, A. L., Beverly Hills, Calif.
Stockwell, E. J., Lexington Park, Md.
Sullivan, L. T., Cambridge, Mass.
Tanner, E. G., Pittsfield, Mass.
Thielking, R. C., North Syracuse, N. Y.
Trexler, R. C., Orange, N. J.
Tyler, R. T., Panorama City, Calif.
Uhlig, W. O., Wharton, N. J.



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Uretz, E. F., Chicago, Ill.
Uses, E. P., Brocton, Mass.
Van Keulen, A. J., Downers Grove, Ill.
Varcoe, R. F., Ottawa, Ont., Canada
Veit, Q. F., Philadelphia, Pa.
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Vuilleumier, R. F., Santa Monica, Calif.
Waite, W. P., Kansas City, Mo.
Walker, J. E., Augusta, Ga.
Walko, D. G., Hollis, L. I., N. Y.
Wasem, E. F., Bloomfield, Conn.
Webb, B. S., Falls Church, Va.
Webb, M. L., Northfield, Vt.
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Wehlander, E. O., Spokane, Wash.
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Werner, M. Haifa, Bat-Galim, Israel
Westbury, R., Fairbanks, Alaska
White, J. V., Whittier, Calif.
Williams, K. F., Dublin, Ireland
Yambor, E. P., Parma, Ohio
Yingst, H. E., Norwalk, Calif.
Zawada, F. A., West Concord, Mass.
Zens, R. G., Natick, Mass.
Zimmerman, H., Forest Hills, L. I., N. Y.
Richie, C. A., Dallas, Tex.

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Andrews, D. S., Toronto, Ont., Canada
Bakaj, E. A., South River, N. J.
Bennett, A. J., Montoursville, Pa.
Berliner, H. J., Washington, D. C.
Beurel, J., Gentilly, Seine, France
Camacho, L.H., Cartagena, Colombia, S. A.
Cavness, R. L., Tustin, Calif.
Cines, S. M., Hicksville, L. I., N. Y.
Conard, L. J., Newburgh, N. Y.
Cunningham, J. A., Cleveland, Ohio
Dalla Volta, E. M., Genoa, Italy
Dupont, W., Tempe, Ariz.
Eckenhoff, W. B., Princeton, N. J.
Edling, D. C., Northridge, Calif.
Evanson, G. L., Anchorage, Alaska
Forest, O. J., Havana, Cuba
George, J. A., Newmarket, N. H.
Gerdes, R. C., Joliet, Ill.
Gibson, C. W., South Boston, Mass.
Goodman, W. D., Dallas, Tex.
Grubel, A. H., New York, N. Y.
Horlick, A. M., North Syracuse, N. Y.
Horvitz, S., Fall River, Mass.
Houston, J. T., Jr., Houston, Tex.
Hunt, J. R., San Francisco, Calif.
Knaff, P. R., Washington, D. C.
Langmuir, D. B., Waltham, Mass.
Lapidus, H. J., Plainview, L. I., N. Y.
Leger, P. P., Albany, Ga.
Le Page, R. W., Willowdale, Ont., Canada
Lindley, R. A., Midwest City, Okla.
Logan, D. J., Chicago, Ill.
Longschein, J. F., Hicksville, L. I., N. Y.
Mac Williams, A. R., Halifax, N. S., Canada
Mc Norton, S. L., Chicago, Ill.
Mimoun, G. L., Puteaux, Seine, France
Mullin, J. L., Los Angeles, Calif.
Neely, O. P., Hinsdale, Ill.
Podhy, R. K., Windsor, Ont., Canada
Prakash, S., Bangalore, India
Ramsey, J. T., Dayton, Ohio
Roberts, M. E., Los Angeles, Calif.
Roberts, W. L., Hickory, N. C.
Sedman, T. M., Gainesville, Va.
Serra, I. C., South Farmingdale, L. I., N. Y.
Smyth, L. E., Compton, Calif.
Storms, W. L., Edmonton, Alta., Canada
Swedberg, P. W., Pacoima, Calif.
Swift, C. W., Encino, Calif.
Thorogood, R. R., Hamilton, Bermuda
Toledo, R. E., Chicago, Ill.
Vargo, F. J., Annandale, Va.
Vinkman, V. V., Farmingdale, L. I., N. Y.
Warner, R. D., Lake Charles, La.
Warren, K. A. J., Danbury, England
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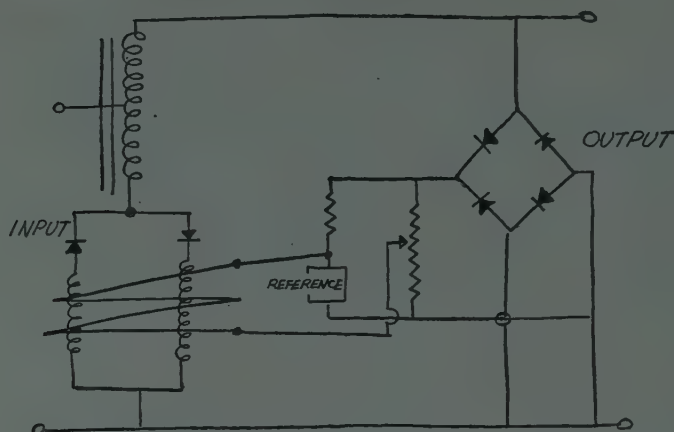
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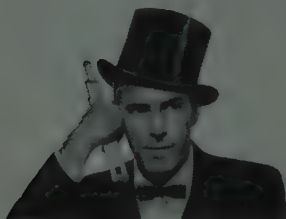
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Section Meetings

AKRON

"Inertial Guidance," L. Lipschultz, Kearfott; 9/16/58.

ALAMOGORDO-HOLLOMAN

"Technical Instructions and Teaching Machines," R. F. Magers, Human Research Unit; 9/15/58.

ANCHORAGE

"Problems of Construction of 'Stretchout' Radar Facilities," J. Dimond, RCA; 10/6/58.

ATLANTA

Tour of Lockheed Aircraft Plant, conducted by R. Ellis and S. R. Smith; 10/3/58.

BALTIMORE

"Management for the Integration of Air Defense System," K. P. Bergquist, U.S.A.F., 9/10/58.

"Future Applications for Electronic Digital Computers," J. W. Mauchly, Remington Rand; 10/8/58.

BAY OF QUINTE

"Basic Measurements and the Radio Engineer," J. T. Henderson, National Research Council; 10/15/58.

CHICAGO

"Future Transistor Materials," A. Coblenz, Ohmite Mfg. Co.; Election of Officers; 5/9/58.

CINCINNATI

"Nike Missile System," R. J. Welsh, USAF; 9/16/58.

DALLAS

"Electronics of the Ultraviolet Flying Spot Television Microscope," W. A. Bonner, U. of Texas S. W. Medical School; "Flying Spot Television Microscope as a Tool in Biological Research," P.O'B. Montgomery, Univ. of Texas S.W. Medical School; 10/7/58.

"Signals from Outer Space and Some Problems Here at Home," Mr. Donald G. Fink, IRE President; 9/2/58.

ELMIRA-CORNING

"New Semiconductor Devices and Applications," A. P. Kruper, Westinghouse Electric Corp.; 9/22/58.

EVANSVILLE-OWENSBORO

"Tactical Air Navigation," A. H. Wulfsberg, Collins Radio Co.; 10/8/58.

FLORIDA WEST COAST

"Radio Frequency Interference and Associated Problems," M. Harges, Empire Device Products; Joint Meeting with PGCS; 9/17/58.

"VORTAC, U. S. Common System Navigational Aid," H. I. Metz, Civil Aeronautics Adm.; Joint with PGANE; Executive Committee Meeting; 10/15/58.

FORT HUACHUCA

"The Engineer and The Wife," F. W. Moorman, U. S. Army; 9/22/58.

FORT WAYNE

"Basic Principles, Circuits and Manufacturing Tests for Transistors," H. R. Lowry, G. E. Co.; 9/4/58.

"The Evolution of the Triode Transistor from Audio to UHF," R. E. Seifert, Philco Corp.; 10/2/58.

FORT WORTH

"Radio Astronomy," G. E. Moreton, Convair Radio Astronomy; 9/23/58.

HAMILTON

"Environmental Simulation and Its Meaning to Electronic Engineers," C. A. Mills, Canadian Westinghouse Co.; Tour of Environmental Labs. and Analogue Computer Center; 9/8/58.

(Continued on page 80A)

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Tung-Sol-developed miniature damper

tubes cut costs of TV manufacture!

New 6AF3 and 12AF3 permit TV set-makers to profit more fully from economies of automated production.

Two new Tung-Sol damper diodes—6AF3 and 12AF3—bring TV manufacturers substantial dollar-savings through increased efficiency. Modern automatic assembly equipment is better able to process the miniature, button-stem dampers than prior octal-base types. Also, the new types allow standardization of tube and socket size—a big plus in printed circuit usage.

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New Tung-Sol miniature dampers compared with types they replace

	BASING	LOAD-RATING	HEATER-RATING
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6AX4GT } 12AX4GTA }	Octal	125ma†	{ 6.3v, 1.2a 12.6v, 0.6a
6AU4GTA } 19AU4GTA }	Octal	190ma†	{ 6.3v, 1.8a 18.9v, 0.6a
12D4	Octal	145ma†	12.6v, 0.6a

*According to Design Maximum System of Ratings
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Section Meetings

(Continued from page 78A)

HAWAII

"IRE Affairs and Related Matters of Interest to Local Section," Mr. Donald G. Fink, IRE President; 8/27/58.

"Missile Instrumentation," R. M. Powell, Lockheed Aircraft; 9/10/58.

HOUSTON

"The Use of the Cathode Ray Tube as a Variable Intensity Section Plotter," R. W. Kelly, Texas Instruments, Inc.; 9/16/58.

HUNTSVILLE

"Air Bearing Gyro Systems," F. W. Kelley, Army Ballistic Missile Agency; 9/23/58.

ITHACA

"Exploration of Terrestrial Space by Radio Waves," W. E. Gordon, Cornell Univ.; Election of new Section Chairman; 10/10/58.

KANSAS CITY

Lecture, Movie & Tour of Sage Installation, Col. Longino, USAF; 9/23/58.

LONG ISLAND

"Alternating Gradient Synchrotron," R. H. Rheaume, Brookhaven National Lab.; 10/14/58.

"Why Space Research," H. York, U. S. Defense Dept.; 10/16/58.

LOS ANGELES

"Mission and Purpose of Pacific Missile Range," J. P. Monroe, Pac. Missile Range; "Development of the Pacific Missile Range," R. F.

Freitag, Pac. Missile Range; Presentation of Awards; 9/9/58.

"Future of Electronics in Pasadena," J. Sheldon, Pasadena Chamber of Commerce; "Report on Moscow IGY Meeting," H. L. Richter, Jet Propulsion Labs.; Presentation of Awards; 10/7/58.

MILWAUKEE

"Signals from Outer Space and Progress at Home," Mr. Donald G. Fink, IRE President; 10/7/58.

NEWFOUNDLAND

"Automatic Electronic Boiler Control," M. Gladden, Nfld. Light & Power Co.; 3/18/58.

"Maintenance of a Tropospheric Scatter System," F. Regni, P.A.F.B.; 4/16/58.

"Ladies' Night"; 4/30/58.
Talk, Mr. Donald G. Fink, IRE President; 6/10/58.

Election Night; 7/2/58.

NORTHERN NEW JERSEY

"Synthetic Music," C. N. Hoyler, RCA; 9/12/58.

"Development of AA Defense," J. Clotz, Institute for Defense Analyses; "Research Activities of the Institute for Defense Analyses," W. R. Hutchins, Institute for Defense Analyses; Joint Meeting with N. J. AIEE; 10/8/58.

NORTHWEST FLORIDA

"Some Aspects of Radio Frequency Interference in Airborne Receivers," M. R. Donaldson, Electronic Communication, Inc.; 8/19/58.

OKLAHOMA CITY

Business Meeting and Tour of Entire Plant of International Crystal Mfg. Co., R. R. Freeland; 10/14/58.

OMAHA-LINCOLN

Tenth Anniversary Celebration; Paper, "Fringe Engineering," T. A. Hunter, Univ. of Iowa; 9/26/58.

(Continued on page 84A)

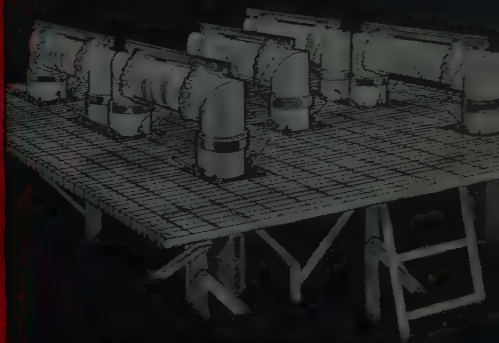


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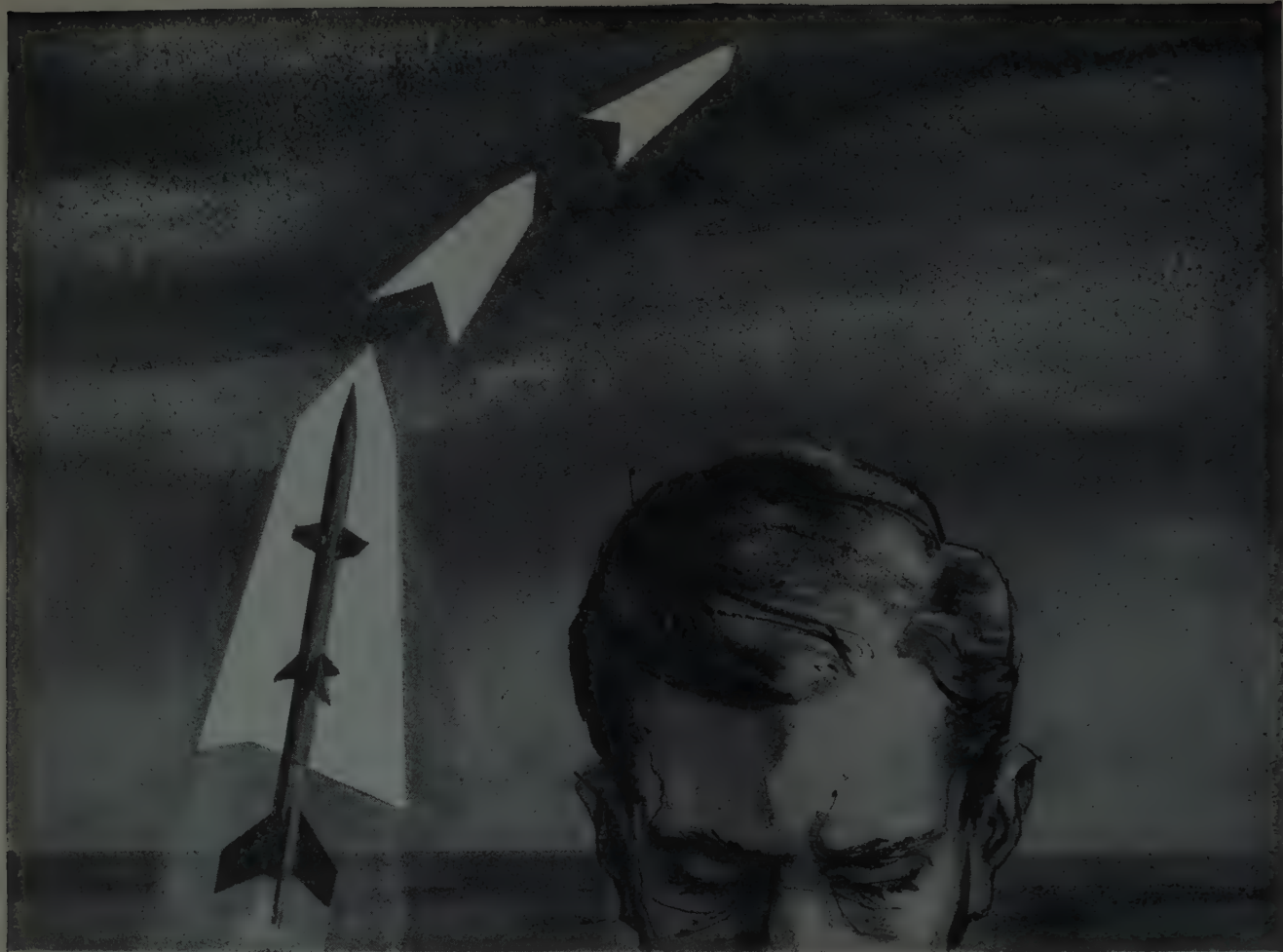
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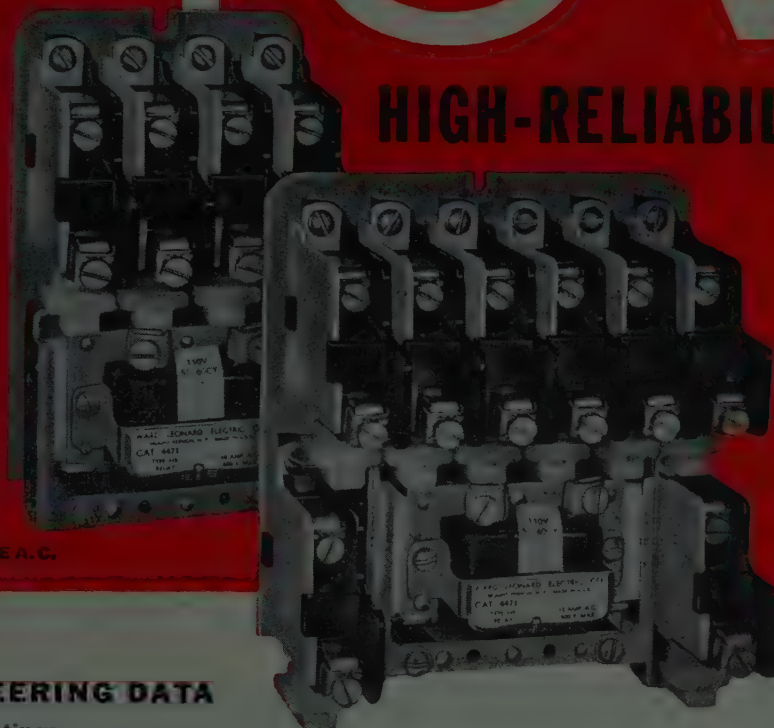
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HIGH-RELIABILITY RELAYS



4 POLE A.C.

- *multi-pole
- *multi-purpose
- *multi-featured

8 POLE A.C.

ENGINEERING DATA

Contact Ratings:

Volts	A.C. Amperes		D.C. Amperes*	
	N.O.	N.C.	N.O.	N.C.
115	10	10	6	5
230	10	10	1	1
440	10	10	—	—
600	10	10	—	—

* Non-inductive resistance loads.

Coils: Standard A.C. coils for 110, 208-220, 440, or 550 volts, 50-60 cycles. Standard D.C. coils for 115 or 230 volts. Other coils on special order.

Poles: 2 to 8, in all combinations of N.O. and N.C. contacts, convertible from N.O. to N.C. and vice versa.

†Dimensions:

A.C.	D.C.	Width	Height	Depth
4 pole	—	3 1/4"	5 1/8"	3 3/32"
8 pole	—	5 1/8"	5 11/16"	3 3/32"
—	4 pole	3 3/8"	5 3/4"	3 3/32"
—	8 pole	5 1/8"	5 3/4"	3 3/32"

† Mounting centers for all models are identical.

Brand new, Type HR solenoid relays are Result-Engineered to function as the "heart" of any control system. The Type HR is designed as a multi-pole relay for piloting machine and process control components where ultra-long life and hi-speed operation are mandatory.

Wiping action contacts insure high electrical reliability; nylon movable contact carriers—separate for each pole—and nylon armature guides minimize operating friction. And, you can add to these features, interchangeable a.c. and d.c. power plants with molded coils.

Simple, fast, easy installation speeds assembly into your equipment, saves time, cuts cost. Accessible front connected coil and contact terminals equipped with pressure connectors . . . no lead lugging needed!

Four basic models with up to eight *unitized* poles maximum; convertible N.O. or N.C. contacts—completely enclosed to keep out dust and foreign particles—make the HR an unusually versatile relay line.

Ask for Ward Leonard Bulletin 4470 for complete technical data. Ward Leonard Electric Co., 35 South Street, Mount Vernon, New York. (In Canada: Ward Leonard of Canada Ltd., Toronto.)

8.6

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MOUNT VERNON, NEW YORK



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RHEOSTATS



RELAYS

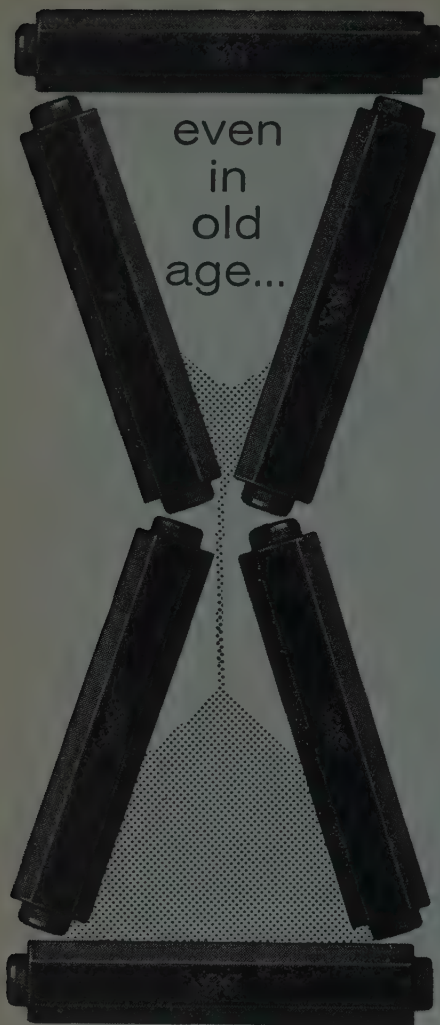


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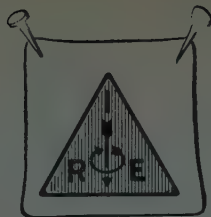
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10,000,000 MEGOHMS!**

65X Molded Resistor 1 watt
80X Molded Resistor 3 watts

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Section Meetings

(Continued from page 80A)

PHOENIX

"Microwave Ferrites," C. L. Hogan, Motorola, Inc.; 9/12/58.

"From Earth to Sun and Beyond, A Rocket Ship Trip to Outer Space," W. Groene, Groene Machine Tool; 10/3/58.

PORTLAND

"Instrumentation Problems in Muscle Action Potentia Research," G. M. Austin, Univ. of Ore. Med. School; 9/18/58.

PRINCETON

"Education for Scientific Engineering," E. Weber, Brooklyn Polytechnic Institute; 10/2/58.

QUEBEC

"Tour of Radio Station"; 9/27/58.

SALT LAKE CITY

"Inertial Guidance," B. Adams, Sperry Utah Engineering Lab.; 10/2/58.

SAN ANTONIO

Business Meeting; 9/19/58.
Demonstration and Tour of IBM Type 705,
R. C. Walz, USAF; 10/16/58.

SAN DIEGO

"Reactor and Control Instrumentation," H. Thomas, General Atomics; 10/7/58.

SAN FRANCISCO

"The Display of Visual Information," M. Rapaport, Stanford Research Institute; Joint Meeting with PGED; 2/12/58.

"Development of Human Engineering Requirements for Information Displays," J. Mangelsdore, Lockheed Missile Systems Div.; Joint Meeting with PGED; 2/19/58.

"Seven Color Radar Display Tube," F. Walcott, Gilfillan Brothers; Joint Meeting with PGED; 2/26/58.

"Direct View Storage Tube," G. Smith, Hughes Aircraft Co.; Joint Meeting with PGED; 3/5/58.

"Sylvatron, a New Application of Electroluminescence," J. W. Waymouth, Sylvania Electric Products, Inc.; Joint Meeting with PGED; 3/12/58.

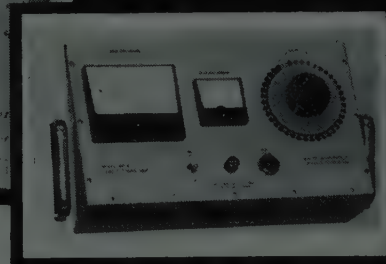
"The Engineer's Interest in Patent Considerations," a Panel Discussion: F. Boxall, Lenkurt Electric; J. Cage, Hewlett Packard; P. Hunter, Varian Associates; J. Ralls, Lippincott; Joint Meeting with PGED; 4/14/58.

"Ceramic Tube Development at Eimac," C. E. Murdock, Eitel-McCullough; "History of Ceramic Tube Development," W. Kohl, Stanford University; Joint with PGED and PGMIL; 6/19/58.

SHREVEPORT

"Single Sideband for Vehicular Communications," D. Land, Motorola Communications & Electronics, Inc.; 10/7/58.

(Continued on page 86A)



MICROWAVE SIGNAL SOURCES ... REMOTELY TUNABLE

Interchangeable R.F. heads covering 1-2KMC, 2-4KMC, 3.6-7.2KMC, 6.7-11.4KMC and 8-14KMC.

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 $\pm 2 \mu$ v, noise less than 0.2 μ v!**

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Above are but a few of the reasons why the new -hp- 425A does the work of complex equipment arrays faster, more simply and with 10 times previous accuracy.

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MICROVOLT-AMPLIFIER

Voltages: Pos. and neg. 10 μ v to 1 v full scale.
11 ranges, 1-3-10 sequence.

Current: Pos. and neg. 10 μ a to 3 ma full scale.
18 ranges, 1-3-10 sequence.

Input Impedance: 1 megohm on voltage ranges,
1 megohm to 0.33 ohms on current ranges.

Accuracy: $\pm 3\%$ full scale.

AMPLIFIER:

Frequency Range: dc to 0.2 cps.

Gain: 100,000 maximum

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Section Meetings

(Continued from page 84A)

SOUTH BEND—MISHAWAKA

"Modern Trends in Scatter Communication—Ionospheric & Tropospheric," P. Rockwell, Page Communications, Inc.; 9/25/58.

TOLEDO

"The Perfect Parallel," a Movie, Libbey-Owens-Ford Glass Co.; "Instrumentation used in the Manufacture of Plate Glass," R. A. Hanna; 9/25/58.

TORONTO

"Slaves, Robots, or Engineers," K. Swinton. Encyclopedia Britannica; 10/9/58.

TUCSON

"Ultrasonics," W. H. Evans, Univ. of Arizona; 9/24/58.

TULSA

"A Demonstration of Stereophonic Equipment," J. Higgins, Magnecord Div. of Midwestern Instruments; 9/25/58.

TWIN CITIES

"Recent Progress in the Use of Balloons as Intermediate Space Vehicles," J. Borth and C. Merell. Gen. Mills, Inc.; 10/6/58.

VIRGINIA

"Satellite Tracking," J. T. Mengel, Naval Research Lab.; 9/19/58.

WESTERN MASSACHUSETTS

"The Future of Science and the Liberal Arts," G. W. Giddings, G. E. Co.; Joint Meeting with W. Mass. Technical Societies; 9/24/58.

WILLIAMSPORT

"Magnetrons in Radar and Other Fields of the Future," F. J. McCarthy, Sylvania Electric Products Inc.; 10/2/58.

SUBSECTIONS

BUENAVENTURA

"New Developments in Telemetry," D. P. Dietz, Radiation, Inc.; 9/10/58.

EASTERN NORTH CAROLINA

"Electronics in Solids, Space and Sound," C. N. Hoyer, RCA; 10/6/58.

GAINESVILLE

"Radio Astronomy," T. D. Carr, Univ. of Fla.; 10/8/58.

LANCASTER

"Reliability through Safety Margin," H. W. Fritz, Army Rocket & Guided Missile Agency, 10/8/58.

MERRIMACK VALLEY

"Science in the Antarctic," D. Linehan, Geophysical Lab. of Boston College; 9/22/58.

MONMOUTH

"Measurement of Voice Circuit Intelligibility by Objective Means," B. T. Newman, Gen. Electronic Labs., Inc.; 9/10/58.

NASHVILLE

"Muscle Potential Amplifiers," L. H. Montgomery, Jr., Vanderbilt Univ. Medical School; 9/24/58.

NORTHERN VERMONT

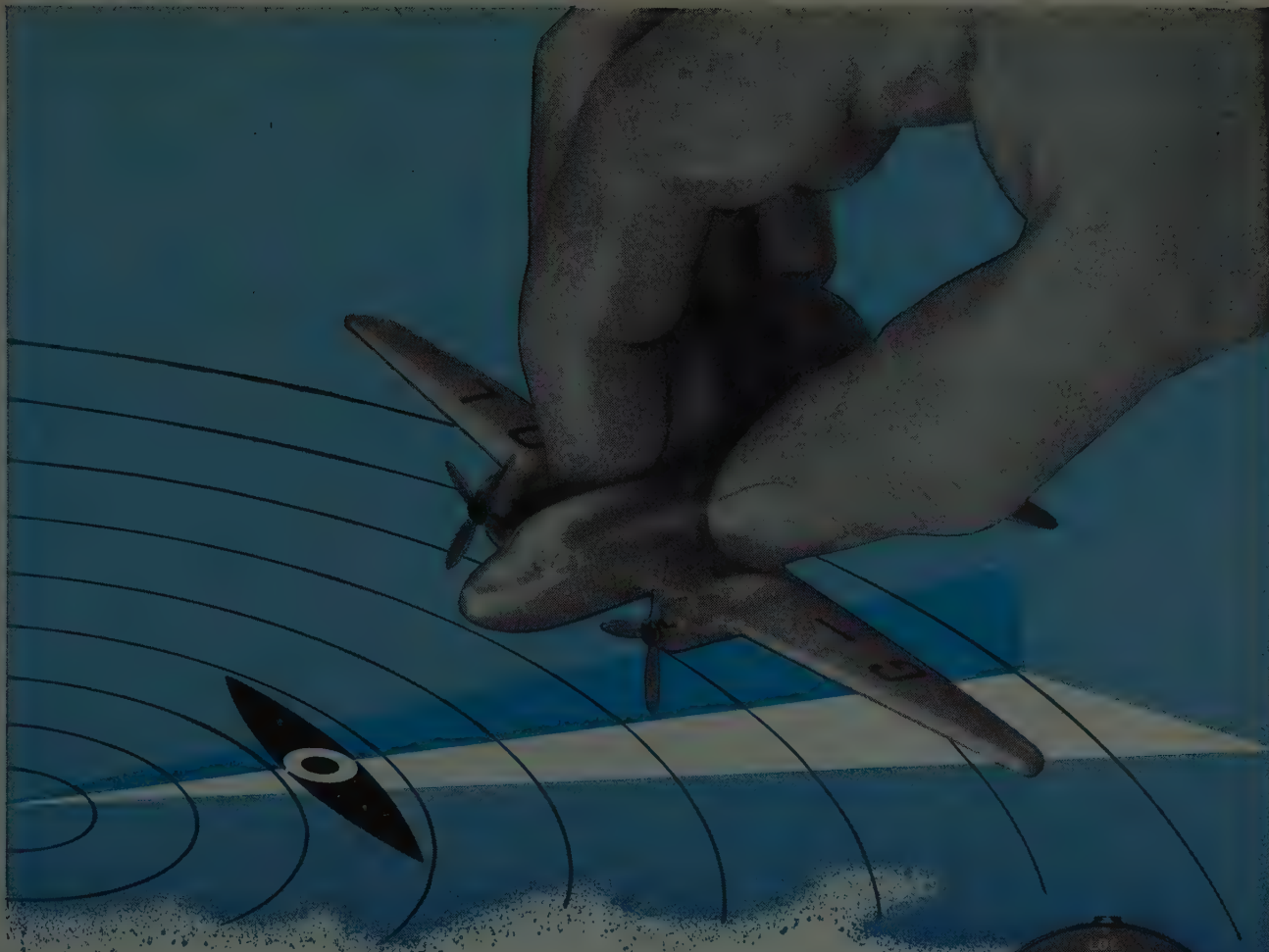
"The Applications of Computers in Commercial and Scientific Fields," G. Stibitz, Consultant; 9/22/58.

PANAMA CITY

"Stereo Sound," B. Shiff, ORRadio Industries, Inc.; 9/23/58.

SAN FERNANDO VALLEY

"Techniques of Modern Brewing," G. C. Voita, Schlitz Brewery; 9/10/58.



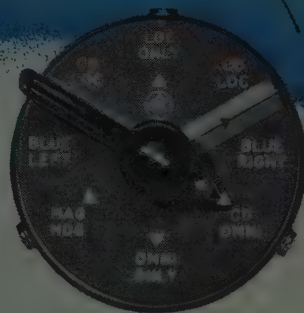
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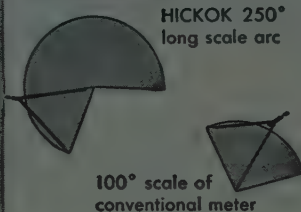
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These instruments meet military specifications and are in volume production. Your inquiry is invited. Kindly list details of your requirements or request Catalog No. 39

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(Continued from page 26A)

Power Supply

The Model HCVS-106-A constant current and constant voltage automatic switchover regulated power supply, manufactured by Matthew Laboratories, 146 Riverdale Ave., Yonkers, N. Y., is designed for the controlled application of Faraday's Law where quantitative coulomb or electric charge transfer or material deposition or removal is to be effected. Some suggested applications are the forming of condensers, controlled and precise electroplating and etching, and other electrolytic processes.



A principal characteristic is the automatic switchover feature. On constant voltage operation, the supply automatically switches to constant voltage operation when the output voltage reaches a selected predetermined value due to buildup of load resistance. The output current range is adjustable from 0 to 20 amperes and the output voltage range is adjustable from 0 to 100 volts. Various control and output current and voltage configurations are available.

Microwave Analyzer

A new microwave analyzer featuring very wide dispersion has been developed by Polarad Electronics Corp., 43-20 34th St., Long Island City 1, N. Y. This unit, Model TSA-W, permits complete visual analysis of extremely narrow to extremely wide microwave pulsed signals in the frequency range 10 to 44,000 mc. For analysis of pulses as short as $0.1 \mu s$, the analyzer provides frequency dispersion up to 70 mc. For wide pulse analysis, the instrument provides a narrower display bandwidth with high resolution (7 kc).

(Continued on page 90A)

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Hughes now makes commercially available a completely reliable single action switch. Used in the Falcon, field proven as a reliable missile, this Hughes relay is engineered to meet the most exacting of requirements.

With unusual speed of action, firing signal triggers the release of constrained contact...contact closes upon fixed contact point...switch circuit becomes permanently closed.

In a typical application, 3.0 volts DC applied to a firing circuit of 1.2 ohms fires within 0.3 seconds.

For additional information please write: Hughes Products, Marketing Department, International Airport Station, Los Angeles 45, California.

SPECIFICATIONS

MECHANICAL—Body Size: Maximum diameter 0.252"; length .920".
Total weight: Less than 0.1 oz.

ELECTRICAL—Before Firing: Insulation resistance is greater than 200 megohms. Minimum breakdown voltage 600 volts.

Firing: 2 volts minimum required. Actual voltage dependent upon closing time desired.

After Firing: Circuit resistance less than 0.3 ohm.

ALTITUDE—Any.

OPERATING TEMPERATURE: -55°C to +125°C.

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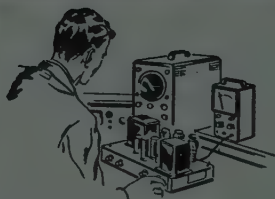
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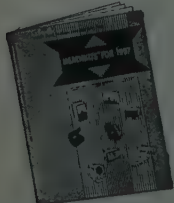
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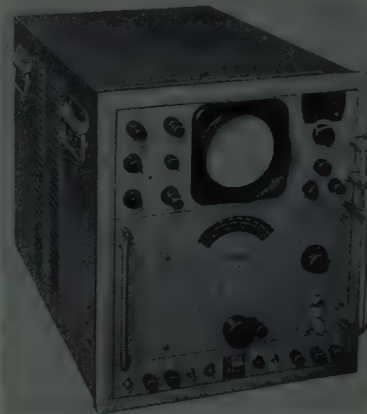
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NEWS New Products



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(Continued from page 88A)



Among the features of this analyzer are a logarithmic amplitude display to accommodate signals within a wide dynamic range; a wide-range marker oscillator calibrated in frequency difference and pulse width; a vernier marker oscillator dial, with stable local oscillators, and non-contacting short-type tuning cavity chokes for long equipment life.

The spectrum is displayed on a cathode-ray tube which has special provision for high intensification for viewing in a brightly-lit room. The frequency range is covered by five sensitive interchangeable plug-in tuning units. Model TSA-W may be used for all microwave spectrum analysis work requiring wide dispersion range, high sensitivity and resolution, such as: observing several signals simultaneously, comparing two signals having relatively small or wide frequency separation, measuring and displaying pulse modulation components, attenuation and band width characteristics, rf leakage and interference, VSWR, and modulator and transmitter malfunctionings.

Erickson Appointed By Servomechanisms

Hawthorne, California: Gerard Q. Decker, Vice President and Division Manager of Servomechanisms, Inc., Subsystems Division, Hawthorne, Calif., has announced the appointment of Thurman C. Erickson to the position of Assistant Division Manager effective August 1, 1958. Erickson was previously Engineering Manager. J. H. Reid, formerly in charge of Electronic Systems Pre-design at the Convair Division of General



(Continued on page 92A)

What the eye would see on the other side of the moon has intrigued and defied the imaginations of scientific minds for centuries. But there's another way to look at moon trips—from a very much down-to-earth point of view. The Space Age is built upon the ingenuity and capabilities of American scientists and engineers who have solved the myriad problems of the space arts—propulsion, stabilization, and control of launching vehicles—and the transmittal, reduction, and analysis of data so that man can comprehend the scientific import of his achievement. The Telecomputing Corporation, through the specialized activities of its six divisions, has contributed significantly to advancements in each of these areas of the space arts. Look to the skills, experience, and facilities of Telecomputing for the solution of your control and data processing problems. Write today for your copy of the TC story—*Empire of Progress*.

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WHITTAKER GYRO Leading producer of electrically driven and spring-wound free gyros, rate and fixed rate gyros for advanced missile systems—rate of roll, pitch, and yaw indicators for manned aircraft—bank and turn indicators.



DATA INSTRUMENTS Pioneers in equipments for fast and accurate analysis of test data, with automatic recording of punched cards, tapes, or printed lists—for aircraft and missile flight tests, industrial and scientific applications.



ENGINEERING SERVICES Specialists in rapid, accurate reduction and evaluation of military and commercial data. Currently handling data reduction for daily missile firings at Holloman Air Force Base.



WHITTAKER CONTROLS The largest developer and builder of custom-built high-performance hydraulic, pneumatic, and fuel valves, controls, and regulators for advanced missile, aircraft, and industrial applications.

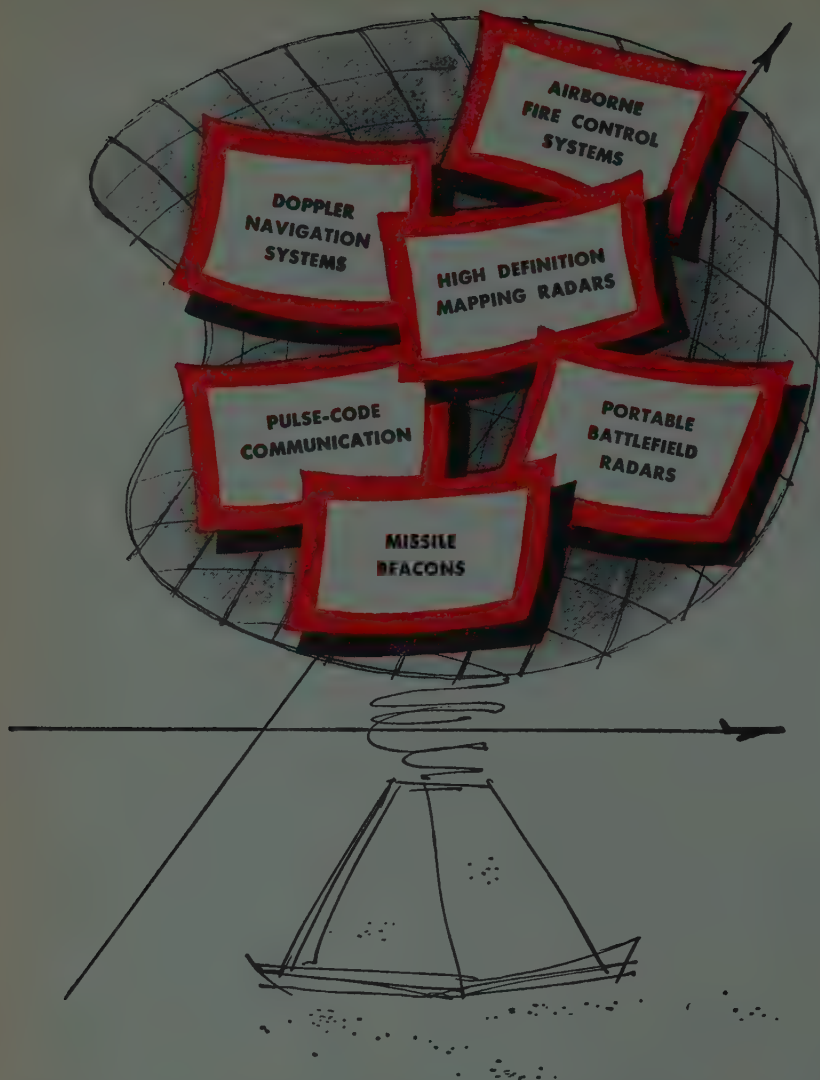


NUCLEAR INSTRUMENTS Designers and builders of high quality, reliable equipments for prelaunch checkout and testing of nuclear special weapons.

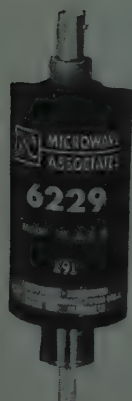
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Which of these radar areas is yours?

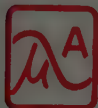


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- HIGH DUTY CYCLE CAPABILITIES
- EXTENDED OPERATING LIFE
- LONG SHELF LIFE

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BURLINGTON, MASSACHUSETTS • BRowning 2-3000



**NEWS
New Products**



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(Continued from page 90A)

Dynamics Corp., has been appointed to the position of Chief Engineer of the Subsystems Division.

Erickson joined SMI in June, 1956, as Industrial Relations Director, a position he held until September 1957 when he was temporarily assigned to the Engineering Department, the post he held until August 1. During his assignment in the Engineering Department, the Eastern Subsystems Engineering Department was consolidated with the Hawthorne Department.

Low-Loss and L-Band Circulator*

By F. R. Arams and G. Krayner, Airborne Instruments Laboratory A. Div. of Cutler Hammer, Inc., Mineola, N. Y.

A four-port circulator, having low insertion loss, has been developed at L-band for use in circulator-maser low-noise receiving systems (reference 1) and other applications. Insertion loss averages 0.3 db over an 18-per cent band (1200 to 1450 mc) when the magnetic field is optimized for each frequency (reference 2). Figure 1

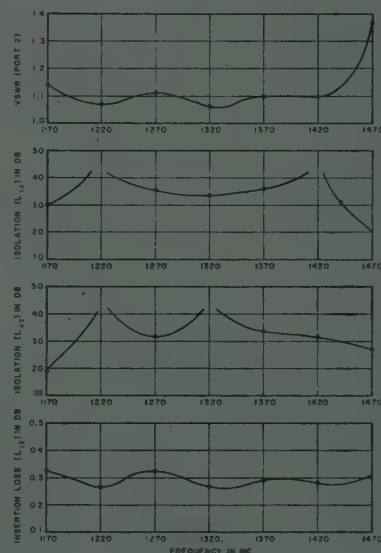


FIGURE 1. PERFORMANCE OF L-BAND CIRCULATOR MODEL 5208-L A1
OPTIMUM MAGNETIC FIELD FOR EACH FREQUENCY

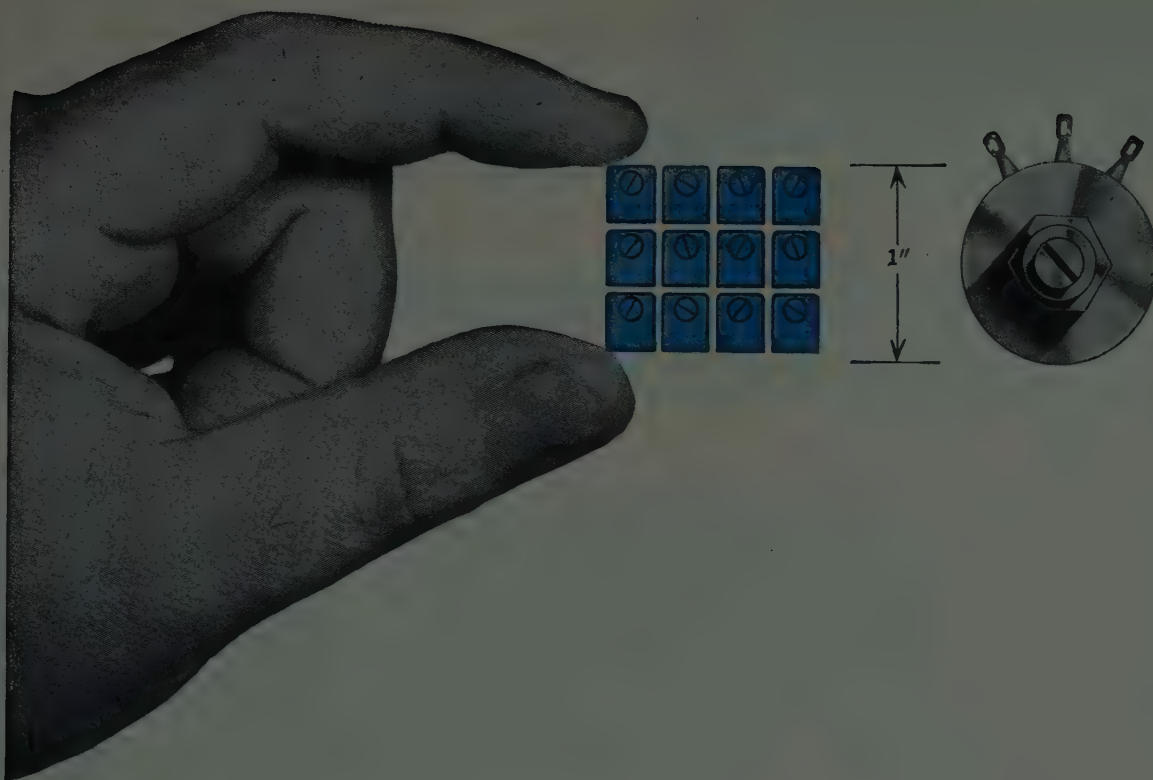
shows the performance of the circulator at the optimum magnetic field for each frequency. The notation L_{xy} used in the graphs denotes the power output measured at circulator port y relative to the power

References

1. F. Arams and G. Krayner, "Design Considerations for Circulator-Maser Systems," Proc. IRE, Vol. 46, p. 912, May 1958; see also Proc. IRE, June 1958, p. 4A.
2. Each 0.1 db of loss corresponds to a noise temperature of about 7 degrees K.

* This work was supported by the Department of Defense

(Continued on page 96A)



FIT 12 OF THESE RECTANGULAR POTENTIOMETERS IN A PANEL AREA OF 1 SQUARE INCH!

You can pack 12 Bourns TRIMPOT® potentiometers in the
1-square-inch area occupied by the average single-turn rotary.

Fit the TRIMPOT into corners—between components—flat against
a chassis or printed circuit board. Mount them individually or in stacked
assemblies. Any way you use them—Bourns potentiometers save space!

You can adjust Bourns potentiometers more accurately, too.

The 25-turn screw-actuated mechanism gives you 9000° of rotation
instead of 270°. Circuit balancing and adjusting is easier, faster.

Repeatability is assured every time. Furthermore, adjustments are
self-locking—shock, vibration and acceleration have no effect!

Write for new Model Summary Brochure

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The G-E Power Tube Microwave Laboratory is located at Stanford Industrial Park, Palo Alto, California where it was one of the Park's pioneer installations. Its scientists and engineers have the advantage of technical exchange with the faculty and research staff of Stanford University, as well as extensive opportunities for graduate training. Constant technical liaison is also maintained with General Electric's own Research and General Engineering Laboratories, Schenectady, N. Y.

HIGH-POWER KLYSTRONS WITH WIDE TUNING ARE DESIGN GOALS OF GENERAL ELECTRIC

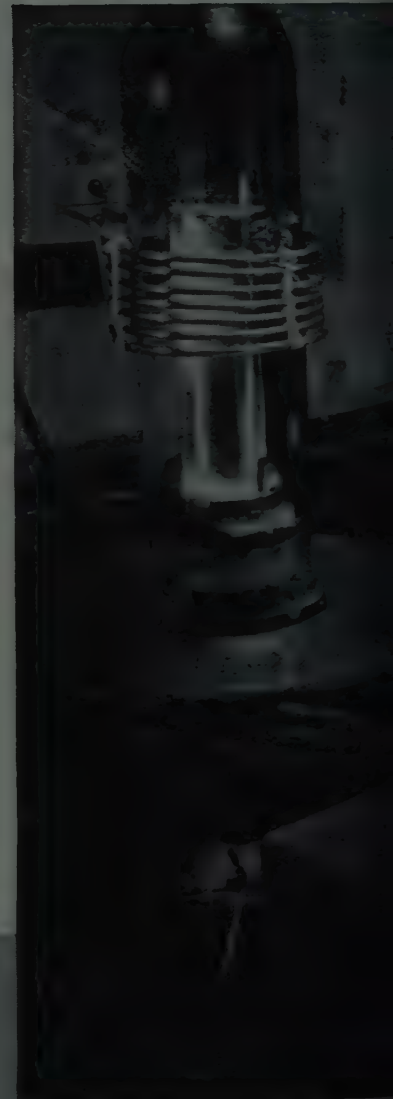
The Microwave Laboratory of the G-E Power Tube Department at Palo Alto, California, is placing major emphasis on the development of a line of advanced-design, high-power klystrons to meet the requirements of radar detection systems and missile guidance systems, as well as navigational equipment of the future.

The requirements for greater operating flexibility, longer life, and higher reliability are being satisfied through the development of klystrons with wider tuning ranges and higher tuning linearity sufficient to enable single-knob control. To achieve wide-range tuning, an exclusive cavity and tuner are employed, consisting of a ring-type tuning vane mechanically coupled to a high-precision single-knob tuning control. Multiple cavity designs and stagger tuning techniques in combination permit broadband operation. The single-knob control permits extremely rapid tuning, while the high tuning linearity permits precise resettability.

Klystron development is only one of a broad range of microwave activities being conducted at the General Electric Microwave Laboratory. Applied research, advanced development, and prototype design are conducted in all areas of microwave tubes and microwave techniques. Technical inquiries pertaining to advanced microwave tube development are invited. *Power Tube Department, General Electric Company, Schenectady, New York.*

* * *

Professional opportunities available for electron tube production, engineering, and scientific personnel. Inquiries are invited.

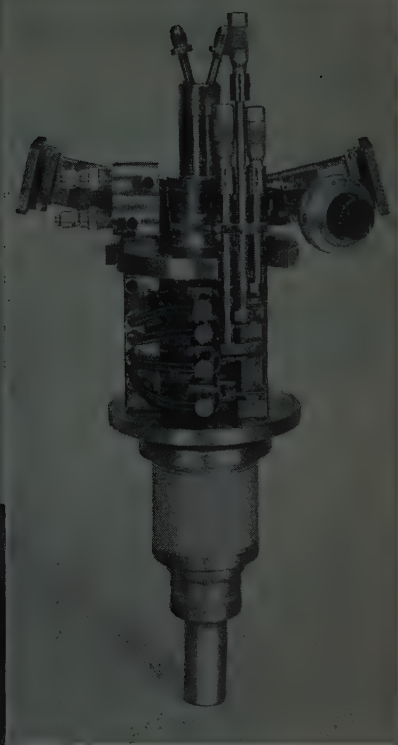


The extensive program of the General Electric Microwave Laboratory on advanced microwave components and techniques includes the following:

CW klystron amplifiers
Super-power klystrons
Voltage-tunable oscillators
High-power duplexers
Microwave filters

Pulse klystron power amplifiers
High-power pulsed TWT amplifiers
Medium-power CW TWT amplifiers
Low-noise, broadband TWT amplifiers
Frequency multiplier TWT amplifiers

ANGES AND HIGH LINEARITY MICROWAVE LABORATORY



▲ Typical of a family of high-power klystrons under development is this 1-KW CW power output tube (solenoid and cover removed) which tunes over a 1000 mc range at X-band, with 40 db gain. All tubes in this family are of rugged, metal-ceramic construction to meet performance standards of military specifications, and employ an extremely long-life, single-knob tuner. Other designs include high-power tubes for L, S and X bands.

◀ Controlled temperature processing of new materials contributes towards improvement in high-emission density cathodes for high-power beam tubes. L. to R., J. F. Kane, consulting engineer, with associates J. N. Lind, D. W. Lashaw and J. P. Fitzpatrick. In foreground, laboratory technician Paul A. Smith.

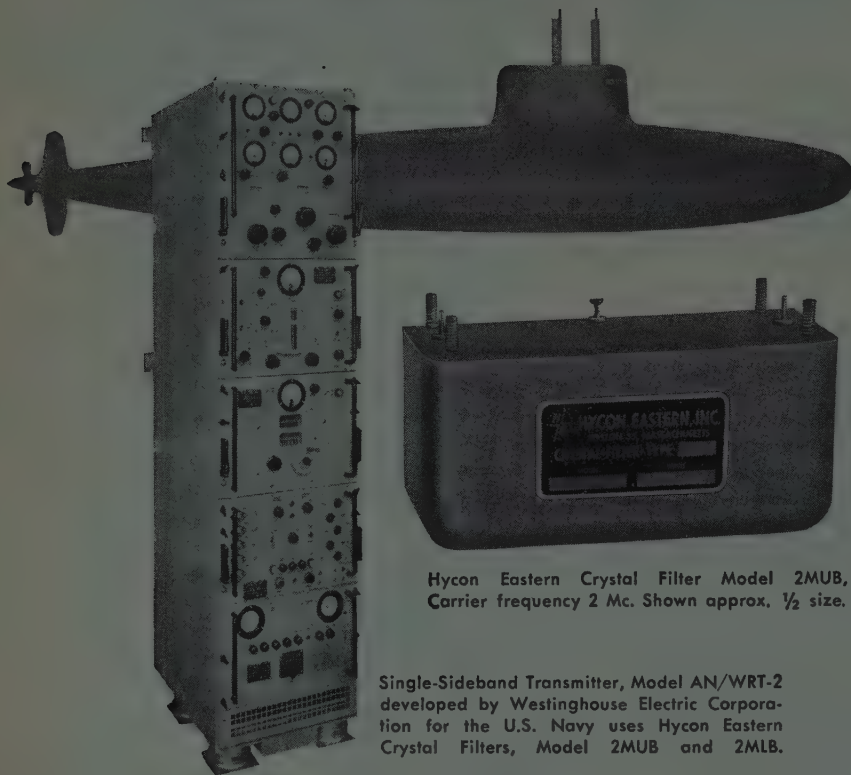
Progress Is Our Most Important Product

GENERAL  ELECTRIC

FIRST Navy Militarized SSB Transmitter

Generates Cleaner Signal Using

HYCON EASTERN CRYSTAL FILTERS



Hycon Eastern Crystal Filter Model 2MUB,
Carrier frequency 2 Mc. Shown approx. 1/2 size.

Single-Sideband Transmitter, Model AN/WRT-2 developed by Westinghouse Electric Corporation for the U.S. Navy uses Hycon Eastern Crystal Filters, Model 2MUB and 2MLB.

Recently installed on the atomic submarine SKIPJACK (SSN585), the Westinghouse Electric AN/WRT-2 SSB Transmitter is soon to be standard Navy equipment.

Single sideband signals are generated in the AN/WRT-2 by the selective filter method employing Hycon Eastern 2MUB and 2MLB Crystal Filters. These 2.0 Mc Crystal Filters not only offer all the basic advantages of the filter SSB generation method, but reduce the number of heterodyning stages required to translate the modulated signal to the required output frequency. The attendant decrease in unwanted signal generation results in a cleaner signal. The AN/WRT-2 is also a more reliable transmitter because fewer components are used.

In addition to the 2.0 Mc Crystal Filters, Hycon Eastern has also supplied SSB units at 100 Kc, 1.75 Mc, 3.2 Mc, 10 Mc and 16 Mc. These Crystal Filters are presently installed in airborne HF, mobile VHF and point to point UHF SSB systems.

Whether your selectivity problems are in transmission or reception, AM or FM, mobile or fixed equipment, you can call on Hycon Eastern engineering specialists to assist you in the design of your circuitry and in the selection of filter characteristics best suited to your needs. Write for Crystal Filter Bulletin to Hycon Eastern, Inc., 75 Cambridge Parkway, Cambridge, Mass.

A limited number of opportunities are available to experienced circuit designers. Send resume to Dr. D. I. Kosowsky.



HYCON EASTERN, INC.

75 Cambridge Parkway

Dept. B

Cambridge 42, Mass.



NEWS New Products



These manufacturers have invited PROCEEDINGS readers to write for literature and further technical information. Please mention your IRE affiliation.

(Continued from page 92A)

input at port x , with all ports terminated in matched loads. Reverse isolation is seen to be ≥ 30 db, and input VSWR is seen to be ≤ 1.11 . The insertion-loss measurement is believed to have an accuracy of better than ± 0.1 db. This measurement was made with padded bolometers that were calibrated against a precision if attenuator.

The ferrite, a magnesium manganese aluminate having a narrow resonance-line width, is operated at a magnetic field above ferromagnetic resonance. An electromagnet is provided to permit magnetic-field adjustment. The circulator is constructed in waveguide that has been substantially reduced in height in the ferrite region to reduce the magnetic-field requirements.

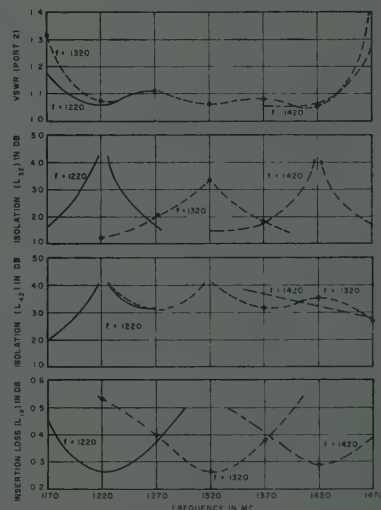


FIGURE 2. PERFORMANCE OF L-BAND CIRCULATOR MODEL 520B-L AT CONSTANT MAGNETIC FIELD, OPTIMIZED FOR 1220, 1320, 1420 MC

Figure 2 shows the performance of the circulator at constant magnetic field optimized for frequencies of 1220, 1320, and 1420 mc. Bandwidth is seen to be about 75 mc for an Isolation $L_{32} \geq 20$ db, with the insertion loss remaining below 0.4 db.

Work on an improved model is in progress.

New Switch

A small lever action switch that would require a minimum depth behind the panel, called Series 12000, is available from Switchcraft, Inc., 555 N. Elston Ave., Chicago 30, Ill.



(Continued on page 98A)

IMPROVED SWITCHING CHARACTERISTICS!

**DELCO HIGH POWER
TRANSISTORS
OFFER UNSURPASSED
PERFORMANCE
FOR HIGH VOLTAGE,
HIGH POWER
APPLICATIONS**



TYPICAL CHARACTERISTICS AT 25°C

	DT100	DT80	2N174A	2N174
Maximum Collector Current	15	15	15	15 amps
Maximum Collector Voltage (Emitter Open)	100	80	80	80 volts
Saturation Resistance	.02	.02	.02	.02 ohms
Thermal Gradient (Junction to Mounting Base)	.8	.8	.8	.8 °C/watt
Nominal Base Current I_B ($V_{EC}=2$ volts, $I_C=5$ amps)	135	100	135	135 ma
Collector to Emitter Voltage (Min.) Shorted Base ($I_C=.3$ amps)	80	70	70	70 volts
Collector to Emitter Voltage Open Base ($I_C=.3$ amps)	70	60	60	60 volts

*Designed to meet MIL-T-19500/13A (Jan) 8 January 1958

**HERE IS A LINE OF TRANSISTORS SPECIALLY
DESIGNED FOR SWITCHING APPLICATIONS.**

Check your switching requirements against the new characteristics of Delco High Power transistors. You will find improved collector to emitter voltage characteristics. You will find higher maximum current ratings—15 amperes. You will find that an extremely low saturation resistance has been retained.

Another important improvement is the solid pin terminal. And, as always, diode voltage ratings are at the maximum rated temperature (95°C.) and voltage.

Write today for engineering data on the new characteristics of all Delco High Power transistors.

DELCO RADIO

Division of General Motors • Kokomo, Indiana

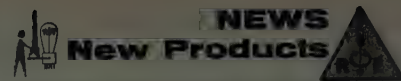
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TWT AMPLIFIERS

P. M. FOCUSED



These manufacturers have invited PROCEEDINGS readers to write for literature and further technical information. Please mention your IRE affiliation.

(Continued from page 96A)

This switch is small in comparative size; single hole mounting; requires $\frac{1}{2}$ of depth of conventional "Key" Switches, behind the panel. It is available in 2 and 3 position types, locking and non-locking, and 3 position locking one side and non-lock other side.

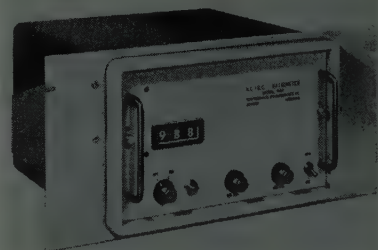
Features include: Relatively long springs without any "forms" at point of flexing insure suitable spring action for long life; easy action with detent "feel" on locking types; Springs assembled into a conventional stack assembly, insulated from each other; fine silver contacts rated at 3 amperes (300 watts maximum) non-inductive load are standard.

Palladium contacts for low-current low-voltage circuits and special circuits are available.

Full information may be had by writing the manufacturer for bulletin S-593.

Digital Ratiometer

A new ac-dc digital ratiometer, model 1594, for computers and control system applications is announced by **Performance Measurements Co.**, 15301 W. McNichols, Detroit 35, Mich. Range of ratios that can be measured directly in numerical values is 0 to 1,000. Input voltages range from 0 to 6.3 volts ac and 0 to 6 volts dc. With a high impedance input, this instrument, measures ac and dc voltage ratios with a rated accuracy of ± 0.10 per cent full scale.



Based on servo null-balance design, the Model 1594 features exceptional freedom from line voltage variations, servo amplifier gain changes, and ambient temperature fluctuations. It also exhibits extremely close follow-up of the signal being measured.

For measuring ac ratios, the digital ratiometer accepts input voltages at a nominal frequency of 400 cps. Frequency variations as high as ± 20 cps and resultant phase shift have no effect on the Ratiometer output reading.

Readability is one part in 1,000. Reference input impedance for both ac and dc ratios is 1,000 ohms. The signal input impedance for the ac section is 20 megohms minimum, and for the dc section it is 10 megohms. Power input is 115 volts, 60 cps and 50 watts.

(Continued on page 104A)



REDUCE WEIGHT AND POWER FOR TWT SYSTEMS BY USING HUGGINS P. M. FOCUSED TUBES.

* COMPARISON OF POWER DISSIPATION AND WEIGHT OF P. M. FOCUSED AND SOLENOID FOCUSED TUBES

FREQ. RANGE	POWER LEVEL	STD. TUBE + SOL. WT.	P. M. TUBE WT.	SOL. + TUBE BEAM POWER	P. M. TUBE BEAM POWER
1.0-2.0 KMC	10 MW	23 LBS.	4.0 LBS.	70 WATTS	0.6 WATTS
2.0-4.0	10 MW	23	4.4	37	1.35
2.0-4.0	1 WATT	25.3	4.5	252	18
4.0-8.0	10 MW	25	4.0	62	1.4
8.0-11.0	10 MW	25	3.6	63	2.4
8.0-11.0	1 WATT	28	4.3	474	44

TUBE TYPE	FREQ. RANGE	HELIX VOLTAGE VOLTS	MAX. CATHODE CURRENT MA.	PRICE*	POWER OUTPUT
HA-31	1.0-2.0 KMC	180-220	4.0	\$1,500.00	10 MW
HA-30	2.0-4.0	800-1100	20.0	1,300.00	1 WATT
HA-29	2.0-4.0	400-525	3.5	975.00	10 MW
HA-28	4.0-8.0	650-800	2.5	1,500.00	10 MW
HA-21	8.2-11.0	2100-2300	20.0	3,000.00	1 WATT
HA-20	8.2-11.0	1200-1300	1.8	1,125.00	10 MW

*QUANTITY DISCOUNTS AVAILABLE ON REQUEST.

HUGGINS LABORATORIES

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Now . . . Ratings > 120 kw
for rectifiers made with
DU PONT SILICON

compact units can eliminate need for dc lines

A wide range of rectifiers made with Du Pont Hyperpure Silicon—with ratings from a few microwatts to > 120 kw per cell—are now available. Manufacturers cite efficiencies up to 99% in units operated at 60 cps, operation at temperatures from -65° to 175°C., rectification ratios as high as 10 million with negligible reverse conductance, and the elimination of special dc lines when these compact rectifiers are used in bridges.

Du Pont, pioneer and first commercial producer of silicon, supplies manufacturers of rectifiers, diodes and transistors with several grades of Hyperpure Silicon. (Du Pont does not produce devices.)

Write today for our free booklet containing full data on Du Pont Silicon: E. I. du Pont de Nemours & Co. (Inc.), 2420 Nemours Bldg., Pigments Department, Wilmington 98, Delaware.



HYPERPURE SILICON

Better Things for Better Living
...through Chemistry

Announcing new

RCA SILICON RECTIFIERS



RCA is now in mass production of silicon rectifiers of the diffused-junction type for use in electronic applications. The two types now available are the initial units of a broad line intended for power supplies of entertainment, industrial, and military equipment.

These RCA Silicon Rectifiers Offer You:

- **Low Cost**—specifically priced for entertainment applications.
- **Electrical Uniformity**—precision controlled diffusion process forms superior junctions.
- **Welded Hermetic Seal**—each unit individually pressure-tested to provide complete protection against moisture and contamination.
- **Rugged Construction**—industrial-type “top-hat” design with axial leads for soldering-in applications; may also be mounted in stand-ard fuse clip.



TYPE	MAXIMUM RATINGS			* CHARACTERISTICS		APPLICATION
	Peak Inverse Volts	RMS Supply Volts	DC Forward Ma	Max. Reverse Current at Indicated Peak Inverse Volts	Max. Instantaneous Forward Voltage at Indicated Instantaneous Forward Current	
1N1763	400	140	500	100 μ a at 400 volts	3 volts at 15 amperes	Black-and-white TV, radios, phonographs and other electronic equipment operating direct from power line
1N1764	500	175	500	100 μ a at 500 volts	3 volts at 15 amperes	Color TV, radios, phonographs and other electronic equipment operating from the power line through a step-up transformer

*At ambient temperature of 25°C

For sales information, contact your RCA Field Representative at any of these offices:

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EAST CENTRAL: 714 New
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RCA Silicon Rectifiers are also available at your local authorized RCA Distributor!

New Designer's Data-Sheets Ready Now!
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RADIO CORPORATION OF AMERICA

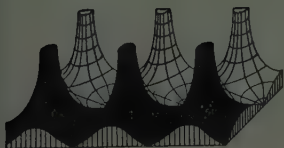
Semiconductor and Materials Division

Somerville, New Jersey

Proceedings of the IRE



Poles and Zeros



Engineering Shortage, 1962?

Passing almost without notice is the fact that last year's college class of freshman engineers

increased only about one per cent over that of 1956. Scattered early reports this fall indicate no significant increase over 1957 and possibly a drop. This does not bode well for the accuracy of predictions which showed our graduations of 1961 and 1962 on an upward trend.

Countering this downward enrollment is a shift to larger electrical engineering enrollments where, under the impact of electronics, many of our departments have made advances in removing the hardware and are attacking the subject at a high science level. Of course you can hear that these boys are attracted to electrical engineering only by the glamor, that the field will not be able to support so many, and they will inevitably return to the older engineering disciplines as more sound and solid. We seem to recall having heard that once before, and isn't electronics now our fifth largest industry?

Good students go where they see the greatest intellectual challenge, and electrical engineering seems to be that field. Another overlooked straw in the wind is that science enrollments generally went up this fall. Does this indicate a greater challenge from the science field to the young student? Do non-electrical branches of engineering appear less glamorous, more stultified, more tied to techniques of this earth than does electrical engineering or science? Has our renovation of engineering education been too long debated and delayed on many campuses, and has it thus placed us in the position of running behind in meeting the desires and aspirations of the good students? Are we going to miss our opportunity and remain a profession of quasi-technicians?

Or does it mean that the electrical engineers are going to have to do the whole job—witness digital computer applications to machine tools or highway cuts and fills (Scanning the *TRANSACTIONS*, page 1972 this issue).

Shows and Symposia. An extensive complex of shows and exhibits, accompanied by technical symposia, has grown up in the electronics profession around IRE sponsorship. Since the first National Electronics Conference in Chicago in 1944 we have added WESCON, NEREM, SWIRECO, MAECON, Dayton PGANE, and others. In recent weeks after attendance at the Cedar Rapids event and NEC, and a near miss at the Canadian Eighth Region Exhibition, we have been impressed with the "taking it to the grass roots" aspects of these services to the electronic profession.

The National Electronics Conference is probably the oldest such event, having just run its fourteenth version. Started in 1944, it already has traditions among which is the story

that it was planned in a cocktail lounge with only fuzzy memories and the minutes on a napkin. After it was swamped with an attendance of 3000 in wartime Chicago after advance preparations for 400, the statement now is that if you stood in line all day for a hotel room, after having confirmed reservations, you are properly a Founder, and if you then slept in the swimming pool you are a Charter Member. The NEC has continued to prosper, and this year had the foresight to sign up in May as a luncheon speaker the man who reciprocated by selecting the NEC weekend to fire the first moon shot that got away—Dr. Simon Ramo.

In operating conferences and shows for service to the profession we have also developed a breed of young volunteer show and convention managers who know how to stage such events properly—who sell the exhibit space, sort the abstracts to find the papers most suited to today's technical interests, sandbag the banquet speakers into speaking, and then start the sessions on time and know how to properly greet and introduce a speaker.

It does not appear that our counterparts in other technical fields have developed these skills in handling guests, nor in conveying apparatus and information to the hinterlands. Perhaps it is the easy portability of much electronics hardware, but we are more inclined to suspect the continuing technical hunger of alert and young scientifically trained minds. The recent shows again contribute to the feeding of these appetites, with improvements in measuring equipment, further sophistication in computing and data handling, and the continuing ascendance of the transistor.

Who attends these symposia and shows? The answer points to the man concerned with technical projects or responsibilities, there to hear papers which will aid him in the solution of his problem, or to find a new Mark II widget, half as large, one fourth as heavy, and ten times as fast as the old 1957 Mark I he has been using. Does he actually attend? Incomplete figures show attendance around the country in excess of 115,000 last year. Considering an IRE membership of 68,000 and a *Fortune* estimate of 100,000 as the electronic engineering population of the country, it seems fair to conclude that these exhibits and programs do serve our profession.

New Members, Anyone? Realizing that an EMF E does not produce a rapid response in circuits of high L , or that an impulse does not instantaneously move a heavy body, or that an application blank is not always to be had when the will to sign is, you will find a membership application ready for filling out and signing following page 6 of the new IRE *DIRECTORY*, so conveniently placed you need not even lift the *DIRECTORY*. —J.D.R.

Elmer H. Schulz

Director, 1958-1959



E. H. Schulz (A'38-SM'46-F'58), assistant director of Armour Research Foundation of Illinois Institute of Technology, was born in Lockhart, Tex., on October 30, 1913. He was graduated from the University of Texas in Austin with the B.S. degree in electrical engineering in 1935 and the M.S. degree in 1936. He received the Ph.D. degree from the Illinois Institute of Technology in Chicago in 1947.

From 1936 to 1942 he taught electrical engineering at the University of Texas. In 1942 he joined the staff of Illinois Institute of Technology, where he taught senior and graduate courses in radio engineering and was in charge of war-training programs in electronics and radio.

He became assistant chairman of the electrical engineering research department of Armour Research Foundation in 1946, and the following year was named chairman of the electrical engineering department. Later he became manager of the

physics and electrical engineering division. His advancement to assistant director of the Foundation in 1953 put him in charge of the research activities of nearly 900 scientists and engineers in nine departments.

He is co-author of "Experiments in Communications and Electronic Engineering," and the author of a number of technical papers. His present position in the IRE is director for the Fifth Region. He served as chairman of the Chicago Section in 1949-1950, and has been on the National Education Committee and the National Industrial Electronics Committee.

Dr. Schulz is a past president of the National Electronics Conference and the Radio Engineers Club of Chicago. He is a Fellow of the American Institute of Electrical Engineers and a member of the Western Society of Engineers and the American Association for the Advancement of Science.

Scanning the Issue

General Power Relationships for Positive and Negative Nonlinear Resistive Elements (Pantell, p. 1910)—Considering the key role that nonlinear devices have long played in radio and electronics, it may seem surprising that our theoretical understanding of nonlinear circuits has not been more fully developed long ago. Although the difficulty of analyzing nonlinear phenomena has caused progress to come slowly, the emergence of more sophisticated devices has provided considerable incentive in recent years for learning more about fundamental properties of nonlinear circuit elements. As a result, a number of important papers have been published on the subject just in the past several years. One of these, which appeared in *PROCEEDINGS* two years ago, investigated some general power relations which govern nonlinear reactance modulators, yielding equations that have proven to be of far-reaching significance in the study of modulators, demodulators, harmonic generators, and parametric amplifiers. The present paper extends this work to include nonlinear resistors, deriving some important relationships concerning modulation efficiency, efficiency of harmonic generation, and stability.

Performance of Some Radio Systems in the Presence of Thermal and Atmospheric Noise (Watt, *et al.*, p. 1914)—This paper presents a wealth of practical communications data that will be of value to engineers concerned with radio systems design and performance specification. The authors examine a large amount of experimental data, both their own and data reported by other workers, for the purpose of comparing the performance of several basic types of communication systems under various typical conditions of fading and noise. The systems studied are aural Morse, frequency shift keying teletype, and voice. From the results of this analysis it now appears possible to predict with a good degree of accuracy the performance of many types of radio systems under a wide range of typical noise conditions. This study should be valuable as a reference in considering the choice of various types of systems, as well as the operating parameters of the system finally selected.

Structure-Determined Gain-Band Product of Junction Triode Transistors (Early, p. 1924)—Ever since the transistor was first developed there has been a good deal of interest in the maximum frequency that could be achieved for amplification and oscillation. The early transistors operated at only a few megacycles. We now have all-transistor equipment that operates at 100 megacycles, and transistors that have been made to oscillate at above 1000 megacycles in the laboratory. This paper describes the upper frequency limit of a diffused base triode transistor in terms of a gain-bandwidth figure of merit that is approximately equal to the maximum frequency of oscillation, and examines what effect the structure of the transistor and the operating biases have on this merit figure. The analysis shows that the diffused base transistor has an upper frequency limit that is an order of magnitude higher than either the field effect or analog transistor, and points an encouraging finger at the possible use of transistors for some microwave applications.

IRE Standards on Audio Techniques: Definitions of Terms, 1958 (p. 1928)—This Standard updates and supersedes a like named Standard issued by the IRE in 1954, covering a subject which represents one of the largest fields of interest (in terms of number of members) within the IRE. It is encouraging to note that despite the fact that radioelectronics is rapidly changing from an empirical art to a highly sophisticated science, its practitioners are still talking in down-to-earth language. Among the 170 terms defined herein one will find

such unpretentious and vividly descriptive words as babble, hiss, hum, singing, and thump. In fact, the only verbal atrocity we could find in its half-dozen pages was one in which radio engineers had no hand in inflicting on a defenseless society: onomatopoeic.

Frequency Variations in Short-Wave Propagation (Ogawa, p. 1934)—If a short-wave transmitter could be built having perfect frequency stability, the signal would nevertheless vary in frequency at the receiving end. The variations would be caused by the up-and-down movement of the reflecting layer of the ionosphere, creating a Doppler effect, and by variations of electron density in the atmosphere, causing changes in propagation velocity. This paper explores the nature and magnitude of these variations and describes experiments in which they were accurately measured. The results are of quite broad interest. For one thing, they emphasize that frequency variations in the short-wave band, where most of the world's standard frequency signals are transmitted, are surprisingly worse than in the VLF band. The magnitude of the variations will also interest communications people, especially those concerned with single sideband systems, where small frequency deviations can cause distortion of the received signal. Finally, the observations provide further insight into the short and long term instabilities and disturbances in the ionosphere itself.

IRE Standards on Recording and Reproducing: Methods of Calibration of Mechanically-Recorded Lateral Frequency Records, 1958 (p. 1940)—It is not unlikely that quite a number of *PROCEEDINGS* readers automatically skip over an IRE Standard when it appears, figuring that it will be about as exciting to read as the dictionary. Actually, these documents, covering as they do the measurement and description of almost every phenomenon and concept in the realm of radio engineering, are very much alive with a rich technical lore that is not only highly instructional but often interesting and unusual as well. This Standard deals with frequency records—records on which various significant frequencies have been recorded in order to test phonograph pickups and recording systems. The purpose of this document is to describe ways of measuring and calibrating the recorded amplitude of the signals impressed in the record. The front cover of this issue hints at the unexpected and ingenious nature of the methods employed. For further details see page 1940.

Annual Indexes to IRE Publications (following p. 1994)—The final 40 pages of the editorial section of this issue provide a key to a major share of the technical developments reported in our field during 1958. In these pages will be found indexes to the titles, authors, and subjects of nearly 1000 papers, letters, and book reviews which appeared in the pages of the *PROCEEDINGS*, the *IRE NATIONAL CONVENTION RECORD*, and the *IRE WESCON CONVENTION RECORD* this year. The 1958 index to the Professional Group *TRANSACTIONS* covering another 800 papers will be published early next year.

An important change has been made this year in the form of the indexes. The author and subject listings, instead of giving a cumulative index number which then has to be looked up in a table of contents to be further identified, refer directly to the month and page number where the item was published.

It might be noted in passing that these final 40 pages bring the number of *PROCEEDINGS* editorial pages published in 1958 to a grand total of 2200, an 18 per cent increase over 1957.

Scanning the *TRANSACTIONS* starts on page 1972.

General Power Relationships for Positive and Negative Nonlinear Resistive Elements*

RICHARD H. PANTELL†, ASSOCIATE MEMBER, IRE

Summary—The method developed by Manley and Rowe for the treatment of nonlinear reactive elements is extended to include nonlinear resistors. General power relationships are derived which yield modulation efficiency, efficiency of harmonic generation, and stability criterion.

INTRODUCTION

MANLEY and Rowe [1] developed some general power relationships for nonlinear reactive elements, and Page [2] considered power relationships for positive nonlinear resistors. The term "positive" implies that $\partial i / \partial v \geq 0$, where i =current, v =voltage, for all values of current and voltage. By means of an approach analogous to the procedure used by Manley and Rowe, it is possible to derive power relationships for positive and negative nonlinear resistors, and to obtain criteria for instability resulting from the presence of a negative nonlinear resistor.

ENERGY RELATIONSHIPS

It is assumed that voltage is a single-valued function of current, and that both the voltage and current associated with the nonlinear resistor of Fig. 1 can be expanded in Fourier series.

Each parallel branch in Fig. 1 is tuned to a different frequency. From left to right, the first branch is the nonlinear resistance, the second branch is tuned to dc, the third branch is tuned to ω_1 , the fourth to ω_0 , and the remaining branches resonate at sum and different frequencies of ω_1 and ω_0 . The Fourier expansions for voltage and current are:

$$v = \sum_{m=-\infty}^{\infty} \sum_{n=-\infty}^{\infty} V_{mn} e^{j(mx+ny)} \quad (1)$$

$$i = \sum_{m=-\infty}^{\infty} \sum_{n=-\infty}^{\infty} I_{mn} e^{j(mx+ny)} \quad (2)$$

$$x = \omega_1 t$$

$$y = \omega_0 t.$$

The dc term is included by letting $m=0=n$.

Since i and v represent real quantities,

$$\begin{aligned} V_{mn} &= V_{-m-n}^* \\ I_{mn} &= I_{-m-n}^* \end{aligned} \quad (3)$$

where the asterisk denotes the complex conjugate. The average real power associated with the mn term is

* Original manuscript received by the IRE, June 23, 1958; revised manuscript received, September 8, 1958.

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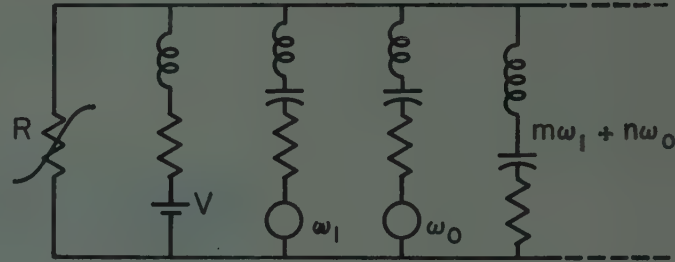


Fig. 1—The multitank nonlinear resistance circuit.

$$\begin{aligned} W_{mn} &= 2 \operatorname{Re}[V_{mn} I_{mn}^*] \\ &= V_{mn} I_{mn}^* + V_{mn}^* I_{mn}. \end{aligned} \quad (4)$$

The reactive power is

$$\begin{aligned} X_{mn} &= 2 \operatorname{Im}[V_{mn} I_{mn}^*] \\ &= j[V_{mn}^* I_{mn} - V_{mn} I_{mn}^*]. \end{aligned} \quad (5)$$

The relationships expressed thus far are the same as those used by Manley and Rowe. In their treatment of the nonlinear resistive element, they proceeded in the following manner. Since

$$V_{mn} = \frac{1}{4\pi^2} \int_0^{2\pi} dy \int_0^{2\pi} dx v e^{-j(mx+ny)} \quad (6)$$

therefore,

$$\begin{aligned} \sum_{m=-\infty}^{\infty} \sum_{n=-\infty}^{\infty} j m V_{mn} I_{mn}^* &= \frac{1}{4\pi^2} \int_0^{2\pi} dy \int_0^{2\pi} dx v \sum_{m=-\infty}^{\infty} \sum_{n=-\infty}^{\infty} j m I_{mn}^* e^{-j(mx+ny)}. \end{aligned} \quad (7)$$

The double summation on the right-hand side of (7) can be expressed in a more convenient form by noting that from (2),

$$\begin{aligned} \frac{\partial i}{\partial x} &= \sum_{m=-\infty}^{\infty} \sum_{n=-\infty}^{\infty} I_{mn} j m e^{j(mx+ny)} \\ &= - \sum_{m=-\infty}^{\infty} \sum_{n=-\infty}^{\infty} I_{mn}^* j m e^{-j(mx+ny)}. \end{aligned} \quad (8)$$

Eq. (9) is obtained by the substitution of (8) in (7):

$$\begin{aligned} \sum_{m=-\infty}^{\infty} \sum_{n=-\infty}^{\infty} j m V_{mn} I_{mn}^* &= - \frac{1}{4\pi^2} \int_0^{2\pi} dy \int_0^{2\pi} dx v \frac{\partial i}{\partial x} \\ &= - \frac{1}{4\pi^2} \int_0^{2\pi} dy \int_{i(0,y)}^{i(2\pi,y)} v di. \end{aligned} \quad (9)$$

Since v is a single valued function of i , and $i(0, y) = i(2\pi, y)$, the right-hand side of (9) is zero. Thus,

$$\begin{aligned} \sum_{m=-\infty}^{\infty} \sum_{n=-\infty}^{\infty} jmV_{mn}I_{mn}^* &= \sum_{m=0}^{\infty} \sum_{n=-\infty}^{\infty} jm(V_{mn}I_{mn}^* - V_{mn}^*I_{mn}) \\ &= \sum_{m=0}^{\infty} \sum_{n=-\infty}^{\infty} mX_{mn} = 0. \end{aligned} \quad (10)$$

Similarly, (11) can be obtained by reversing the order of integration in (6),

$$\sum_{m=-\infty}^{\infty} \sum_{n=0}^{\infty} nX_{mn} = 0. \quad (11)$$

Eqs. (10) and (11) are valid, but yield little useful information regarding the behavior of nonlinear resistors.

The procedure that follows gives relationships involving real power rather than reactive power. First, both sides of (6) are multiplied by $-m^2I_{mn}^*$ and summed over m and n , as expressed by (12):

$$\begin{aligned} \sum_{m=-\infty}^{\infty} \sum_{n=-\infty}^{\infty} -m^2V_{mn}I_{mn}^* \\ = \frac{1}{4\pi^2} \int_0^{2\pi} dy \int_0^{2\pi} dx v \sum_{m=-\infty}^{\infty} \sum_{n=-\infty}^{\infty} -m^2I_{mn}^* e^{-j(mx+ny)}. \end{aligned} \quad (12)$$

Since

$$\begin{aligned} \frac{\partial^2 i}{\partial x^2} &= \sum_{m=-\infty}^{\infty} \sum_{n=-\infty}^{\infty} -m^2I_{mn} e^{j(mx+ny)} \\ &= \sum_{m=-\infty}^{\infty} \sum_{n=-\infty}^{\infty} -m^2I_{mn}^* e^{-j(mx+ny)}, \end{aligned} \quad (13)$$

(12) can be rewritten in the form given by (14):

$$-\sum_{m=-\infty}^{\infty} \sum_{n=-\infty}^{\infty} m^2V_{mn}I_{mn}^* = \frac{1}{4\pi^2} \int_0^{2\pi} dy \int_0^{2\pi} dx v \frac{\partial^2 i}{\partial x^2}. \quad (14)$$

The right-hand side of (14) can be integrated by parts:

$$\begin{aligned} \frac{1}{4\pi^2} \int_0^{2\pi} dy \int_0^{2\pi} dx v \frac{\partial^2 i}{\partial x^2} \\ = \frac{1}{4\pi^2} \int_0^{2\pi} dy \left[v \frac{\partial i}{\partial x} \Big|_0^{2\pi} - \int_0^{2\pi} dx \frac{\partial v}{\partial x} \frac{\partial i}{\partial x} \right]. \end{aligned} \quad (15)$$

Because of the periodicity of v and i ,

$$v \frac{\partial i}{\partial x} \Big|_0^{2\pi} = 0.$$

Also,

$$\int_0^{2\pi} dx \frac{\partial v}{\partial x} \frac{\partial i}{\partial x} = \int_0^{2\pi} dx \frac{\partial i}{\partial v} \left(\frac{\partial v}{\partial x} \right)^2.$$

With the above equalities substituted for the right-hand side of (14), (16) is obtained:

$$\begin{aligned} \sum_{m=-\infty}^{\infty} \sum_{n=-\infty}^{\infty} m^2V_{mn}I_{mn}^* \\ = \frac{1}{4\pi^2} \int_0^{2\pi} dy \int_0^{2\pi} dx \frac{\partial i}{\partial v} \left(\frac{\partial v}{\partial x} \right)^2. \end{aligned} \quad (16)$$

Since

$$\begin{aligned} \sum_{m=-\infty}^{\infty} \sum_{n=-\infty}^{\infty} m^2V_{mn}I_{mn}^* &= \sum_{m=0}^{\infty} \sum_{n=-\infty}^{\infty} m^2[V_{mn}I_{mn}^* + V_{mn}^*I_{mn}] \\ &= \sum_{m=0}^{\infty} \sum_{n=-\infty}^{\infty} m^2W_{mn}, \end{aligned}$$

the desired power relationship is:

$$\sum_{m=0}^{\infty} \sum_{n=-\infty}^{\infty} m^2W_{mn} = h_m, \quad (17)$$

where

$$h_m = \frac{1}{4\pi^2} \int_0^{2\pi} dy \int_0^{2\pi} dx \frac{\partial i}{\partial v} \left(\frac{\partial v}{\partial x} \right)^2. \quad (18)$$

If the order of integration is reversed in (6), (19) may be obtained by the same procedure used to derive (17):

$$\sum_{m=-\infty}^{\infty} \sum_{n=0}^{\infty} n^2W_{mn} = h_n, \quad (19)$$

where

$$h_n = \frac{1}{4\pi^2} \int_0^{2\pi} dx \int_0^{2\pi} dy \frac{\partial i}{\partial v} \left(\frac{\partial v}{\partial y} \right)^2. \quad (20)$$

The power relationships expressed by (17) and (19) define the characteristics of the nonlinear resistive element.

THE POSITIVE NONLINEAR RESISTOR

The positive resistor has the characteristic that $\partial i / \partial v \geq 0$, which means the integrands in (18) and (20) are never negative. Therefore the power relationships can be written as

$$\sum_{m=0}^{\infty} \sum_{n=-\infty}^{\infty} m^2W_{mn} \geq 0 \quad (21)$$

$$\sum_{m=-\infty}^{\infty} \sum_{n=0}^{\infty} n^2W_{mn} \geq 0. \quad (22)$$

For the case of harmonic generation this means that

$$\frac{W_{m0}}{W_{10}} \leq \frac{1}{m^2}$$

where

W_{10} = power associated with the local oscillator frequency

W_{m0} = power associated with the m th harmonic.

This result is the same as that obtained by Page [2]. For the case where modulation is involved (23) and (24) are obtained:

$$W_{10} + m^2 W_{mn} \geq 0 \quad (23) \quad \text{where}$$

$$W_{01} + n^2 W_{mn} \geq 0 \quad (24) \quad \left(\frac{\partial v}{\partial y} \right)^2$$

where

W_{10} = power associated with the local oscillator frequency

W_{01} = power associated with the signal frequency

W_{mn} = power associated with the modulation frequency.

Since the coefficient of W_{mn} is positive in both (23) and (24), instability is not possible in the manner that instability might result for the nonlinear reactive element. In addition, power is not conserved. Since

$$P_{in} = W_{10} + W_{01}$$

$$P_{out} = |W_{mn}|,$$

the conversion efficiency is

$$\eta = \frac{P_{out}}{P_{in}} \leq \frac{1}{m^2 + n^2}.$$

For $m=n=1$, the maximum conversion efficiency is 50 per cent. For frequency doubling by means of harmonic generation the maximum efficiency is 25 per cent.

Eqs. (17) and (19) are valid for a linear resistor. For this case

$$\frac{\partial i}{\partial v} = G = \text{constant},$$

and h_m and h_n become

$$h_m = 2G \sum_{m=0}^{\infty} \sum_{n=-\infty}^{\infty} m^2 V_{mn} V_{mn}^*$$

$$h_n = 2G \sum_{m=-\infty}^{\infty} \sum_{n=0}^{\infty} n^2 V_{mn} V_{mn}^*.$$

Since $W_{mn} = 2G V_{mn} V_{mn}^*$, this means that all the power into the resistor at each frequency is dissipated as loss and there can be no harmonic generation or modulation.

SMALL-SIGNAL ANALYSIS

If the local oscillator voltage is much larger than the signal and modulation voltages, then $\partial i / \partial v$ is a periodic function of x only:

$$\frac{\partial i}{\partial v} = \sum_{r=-\infty}^{\infty} G_r e^{j r x}. \quad (25)$$

Since $\partial i / \partial v$ is a real quantity,

$$G_{-r} = G_r^*.$$

The expression for h_n is

$$h_n = \frac{1}{4\pi^2} \int_0^{2\pi} dx \sum_{r=-\infty}^{\infty} G_r e^{j r x} \int_0^{2\pi} dy \left(\frac{\partial v}{\partial y} \right)^2, \quad (26)$$

$$= \sum_{q=-\infty}^{\infty} \sum_{r=-\infty}^{\infty} \sum_{m=-\infty}^{\infty} \sum_{n=-\infty}^{\infty} V_{qr} V_{mn} (-jn) e^{j[(m+q)x + (n+r)y]}.$$

Because of the orthogonality of the exponential functions over the period 2π ,

$$\int_0^{2\pi} \left(\frac{\partial v}{\partial y} \right)^2 dy = 2\pi \sum_{q=-\infty}^{\infty} \sum_{r=-\infty}^{\infty} \sum_{n=-\infty}^{\infty} n^2 V_{qn}^* V_{mn} e^{j(m-q)x}.$$

Therefore h_n becomes

$$h_n = \frac{1}{2\pi} \int_0^{2\pi} dx \sum_{r=-\infty}^{\infty} \sum_{q=-\infty}^{\infty} \sum_{m=-\infty}^{\infty} \sum_{n=-\infty}^{\infty} n^2 G_r V_{qn}^* V_{mn} e^{j(m-q+r)x}$$

$$= \sum_{q=-\infty}^{\infty} \sum_{m=-\infty}^{\infty} \sum_{n=-\infty}^{\infty} n^2 G_{(q-m)} V_{qn}^* V_{mn}. \quad (27)$$

The notation $G_{(q-m)}$ does not mean a double index on G , but rather that the G_r appearing in Eq. (27) corresponds to $r=q-m$. The small-signal power relationship is

$$\sum_{m=-\infty}^{\infty} \sum_{n=0}^{\infty} n^2 W_{mn} = \sum_{q=-\infty}^{\infty} \sum_{m=-\infty}^{\infty} \sum_{n=-\infty}^{\infty} n^2 G_{(q-m)} V_{qn}^* V_{mn}$$

$$G_{(q-m)} = \frac{1}{2\pi} \int_0^{2\pi} dx \frac{\partial i}{\partial v} e^{-j(q-m)x}. \quad (28)$$

If the external circuit is adjusted so that only the signal frequency and the modulation frequency corresponding to $m=1=n$ face an appreciable impedance, (28) becomes

$$W_{01} + W_{11} = 2G_0[V_{01}^* V_{01} + V_{11}^* V_{11}]$$

$$+ 2G_{-1}V_{11}V_{01}^* + 2G_1V_{01}V_{11}^*. \quad (29)$$

By an appropriate choice for the $x=0$ axis for the function $\partial i / \partial v$, it is possible to make

$$G_{-1} = G_1^* = G_1 = \text{a real constant}.$$

For this choice, (29) may be written as

$$W_{01} + W_{11} = 2G_0[|V_{01}|^2 + |V_{11}|^2]$$

$$+ 2G_1[V_{11}V_{01}^* + V_{01}V_{11}^*]. \quad (30)$$

If instability is to occur it is necessary that

$$2G_0[|V_{01}|^2 + |V_{11}|^2] + 2G_1[V_{11}V_{01}^* + V_{01}V_{11}^*] < 0.$$

Since

$$|V_{01}|^2 + |V_{11}|^2 \geq V_{11}V_{01}^* + V_{01}V_{11}^*,$$

the necessary conditions for instability are [3]

$$\left. \begin{aligned} G_0 &< 0 \\ G_0^2 - G_1^2 &< 0. \end{aligned} \right\} \quad (31)$$

EQUIVALENT CIRCUIT

Eq. (28), which applies for the small-signal condition [4], may be derived in a somewhat different manner by noting that

$$\begin{aligned}\Delta i &= \frac{\partial i}{\partial v} \Delta v \\ &= \sum_{r=-\infty}^{\infty} G_r e^{irx} \Delta v,\end{aligned}\quad (32)$$

where

$$\left. \begin{aligned}\Delta i &= \sum_{m=-\infty}^{\infty} \sum'_{n=-\infty}^{\infty} I_{mn} e^{j(mz+ny)} \\ \Delta v &= \sum_{m=-\infty}^{\infty} \sum'_{n=-\infty}^{\infty} V_{mn} e^{j(mz+ny)}\end{aligned}\right\} \quad (33)$$

The prime on the summation over n indicates that the $n=0$ term is not included, and therefore Δi and Δv involve only the signal frequency and the modulation terms. Combining (32) and (33), I_{mn} may be written as

$$I_{mn} = \sum_{q=-\infty}^{\infty} G_{m-q} V_{qn}. \quad (34)$$

By taking the complex conjugate of (34), multiplying by $n^2 V_{mn}$, and then summing over m and n , (28) results. Assuming only the presence of the signal and one modulation frequency corresponding to $m=n=1$, (35) and (36) result:

$$I_{01} = G_0 V_{01} + G_1 V_{11} \quad (35)$$

$$I_{11} = G_1 V_{01} + G_0 V_{11}. \quad (36)$$

In terms of usual network notation, G_0 and G_1 correspond to the short-circuit admittance parameters, and

(31) specifies the condition for non-physical realizability by means of passive elements. A π -network may be used for realization as illustrated in Fig. 2. It is interesting to note that reciprocity holds for the nonlinear resistance, whereas this is not true for the nonlinear reactance. For any specified problem where the driving sources and associated impedances are given, gain and bandwidth may be determined by ordinary network calculations by connecting the sources and impedances to the appropriate terminals of Fig. 2 [4].

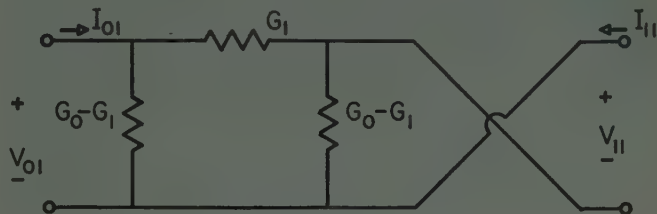


Fig. 2—Small signal equivalent circuit for the nonlinear resistance.

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CORRECTION

G. L. Turin, author of "Error Probabilities for Binary Symmetric Ideal Reception through Nonselective Slow Fading and Noise," which appeared on pages 1603-1619 of the September, 1958, issue of *PROCEEDINGS*, has requested that the following corrections be made to his paper.

The first line of (12) on page 1606 should read:

$$\rho_m(u) = \frac{1}{2} \int \xi^*(t) \xi_m(t - u) dt.$$

A factor of t should be inserted in the integrand of (17) on page 1607.

In the first column of page 1609, the thirteenth line from the top should begin: Since $\gamma = 2 \dots$

The line immediately following (54b) on page 1612

should read: and similar expressions hold for $\hat{v}(t)$ and $\bar{v}(t)$. On the following page, the right-hand sides of (56) and (57) should be $\bar{\mu}(t)$ and $\bar{v}(t)$, respectively.

On page 1614, on the next to last line of section B, the m should be a subscript to the x .

In (84), on page 1615, the right-hand side of the last equation should be $2\lambda EN_0$.

In some copies, (103) and (106) on page 1617 were printed incorrectly. The first factor on the right-hand side of (103) should read $e^{(x^2+y^2)/2}$. The first factor in the second line of (106) should be $e^{-\beta a^2/4\sigma^2}$.

The second equation of (118) should read:

$$K_2 = \frac{B}{1 - B^2}.$$

Performance of Some Radio Systems in the Presence of Thermal and Atmospheric Noise*

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E. L. MAXWELL†, AND R. W. PLUSH†

Summary—The performance of several basic types of communication systems are determined experimentally, and in some cases theoretically, under typical conditions with steady or fading carriers, and in the presence of thermal or atmospheric noise. The relative efficiency of various carriers and the interference factor of various types of noise are found to be dependent upon the characteristics of the particular communication system as well as the characteristics of the carrier and noise themselves.

Methods are considered for calculating errors expected from a given system, based upon the amplitude distribution of the noise envelope.

INTRODUCTION

A COMPLETE radio communication system can be considered as consisting of a large number of independent circuit elements arranged in a manner similar to that shown in Fig. 1. In general, the objectives are to have a system capable of reproducing a given class or type of message at a given rate of transmission with maximum reliability. At the same time, it is essential that the system require a minimum amount of transmitter power and produce a minimum amount of interference to services in adjacent channels. The accomplishment of these ends requires a careful consideration of the characteristics of all parts of the system and their interrelated effects.

Fig. 1 illustrates the interesting fact that there are two system elements, the propagation path and the atmospheric noise, whose characteristics are beyond our control. In view of this, it is readily apparent that the characteristics of these two system elements must be determined as thoroughly as possible so that the other elements can be designed for optimum operation under the conditions established by the propagation path and the limiting noise.

CARRIER CHARACTERISTICS

The carrier characteristics are functions of many parameters, including path distance, terrain, frequency, and antennas. In general, VLF and LF carriers are nonfading, *i.e.*, have a steady amplitude for normal message periods. HF carriers as a rule, are steady for ranges where propagation is by ground wave but are subject to ionospheric fading and multipath conditions at other ranges. VHF and UHF carriers also are relatively steady for short ranges, but have appreciable fading for beyond-horizon circuits.

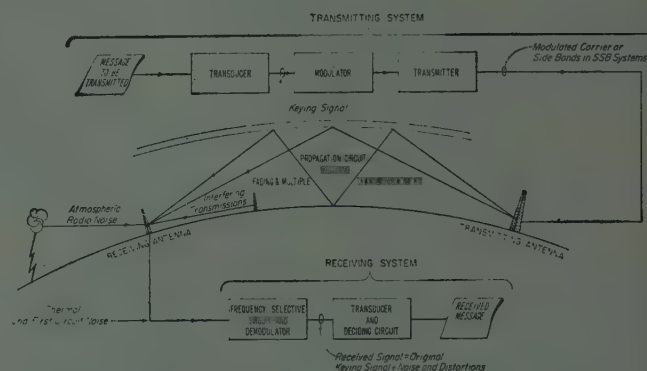


Fig. 1—Diagram of a typical radio communication system.

Long-range HF carriers frequently have a variation in amplitude which can be considered as resulting from the combination of a specularly reflected component and a number of scattered contributions. McNicol¹ has shown how the resulting envelope amplitude distribution may vary from a primarily Rayleigh distribution to that of a Gaussian distribution depending, of course, on the relative amount of specular and scattered components. The actual shape of the distribution at a particular time naturally will influence the efficiency of the carrier in transferring information. The rate of variation is also an important factor in determining the errors which will be introduced by fading on specific radio systems. The average fade rate varies considerably with propagation conditions and usually is within the range of 1/10 to 10 fades per second.

Norton, *et al.*,² Bullington, *et al.*,³ and Chisholm, *et al.*,⁴ have shown that the carriers received over typical beyond-horizon UHF paths have instantaneous envelope amplitude distributions which at times approximate the Rayleigh distribution, but also are seen to depart appreciably from this distribution.

Recent measurements of the 1046-mc radiation from Cheyenne Mountain, Colo., to Garden City, Kan., have been made with equipment which determines directly

¹ R. W. E. McNicol, "The fading of radio waves of medium and high frequencies," *Proc. IEE*, vol. 96, pt. III, pp. 517-524; November, 1946. (See also footnote 18.)

² K. A. Norton, P. L. Rice, H. B. Janes, and A. P. Barsis, "The rate of fading in propagation through a turbulent atmosphere," *Proc. IRE*, vol. 43, pp. 1341-1353; October, 1955.

³ K. Bullington, W. J. Inkster, and A. L. Durkee, "Results of propagation tests at 505 mc and 4,090 mc on beyond-horizon paths," *Proc. IRE*, vol. 43, pp. 1306-1316; October, 1955.

⁴ J. H. Chisholm, P. A. Portman, J. T. deBettencourt, and J. F. Roche, "Investigations of angular scattering and multipath properties of tropospheric propagation of short radio waves beyond the horizon," *Proc. IRE*, vol. 43, pp. 1317-1335; October, 1955.

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† National Bureau of Standards, Boulder, Colo.

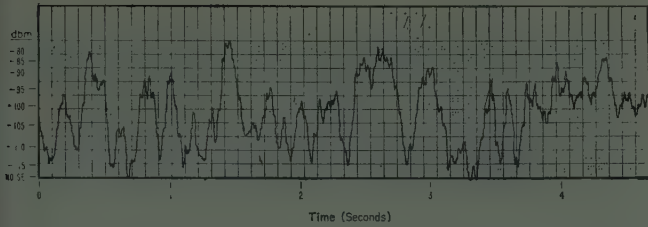


Fig. 2—Forward scatter tropospheric signal envelope, Cheyenne Mountain, Colo., to Garden City, Kan., 226 miles. Carrier frequency 1046 mc, recorder response dc to 40 cps (3 db down), 0619 MST, March 7, 1957.

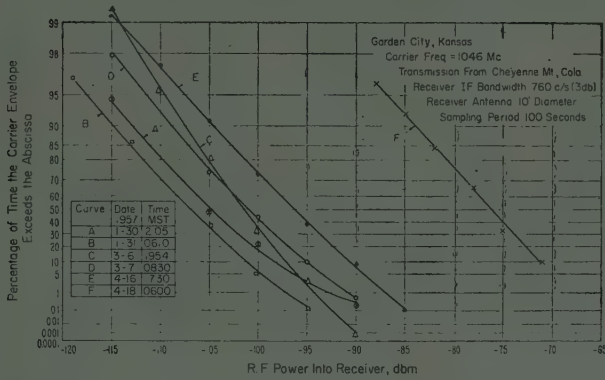


Fig. 3—Cumulative distribution of carrier envelope amplitudes.

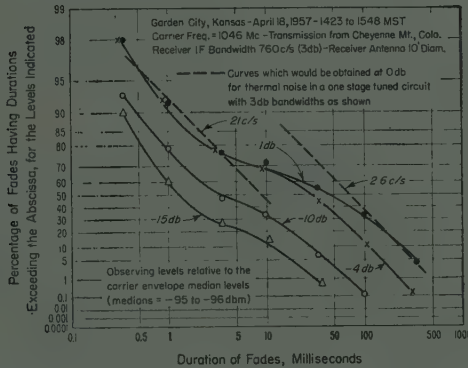


Fig. 4—Cumulative distribution of carrier fade lengths at various levels.

the cumulative distribution of the instantaneous envelope of the receiver IF output. In addition to these direct measurements of the amplitude and time distributions with equipment similar to that described elsewhere^{5,6} recordings were made simultaneously with a high-speed recorder whose frequency response is from dc to 3 db down at 40 cps. A short portion of the record is shown in Fig. 2, which gives some indication of the type of field fluctuation encountered. The amplitude distributions seen in Fig. 3 were obtained directly with electronic cumulative distribution circuitry with a resolving capability of less than 0.1 millisecond where it

⁵ E. F. Florman, R. W. Plush, A. D. Watt, C. F. Peterson, and A. F. Barghausen, "Some measured statistical characteristics of a 1046mc carrier over a tropospheric scatter radiolink," in preparation.
⁶ A. D. Watt and E. L. Maxwell, "Measured statistical characteristics of VLF atmospheric radio noise," *Proc. IRE*, vol. 45, pp. 55-62; January, 1957.

can be seen that the instantaneous envelope amplitude is not always Rayleigh distributed. The sampling period for the simultaneously obtained data points of Fig. 3 was 100 seconds, while the data for each of the time distribution curves of Fig. 4 required approximately 10 minutes. It should be mentioned that other observations of time distributions indicate that appreciable changes in the rate of fading do occur over such paths.

Observation of the fade durations of thermal noise through a narrow-band filter has yielded results similar to that shown in Fig. 4 except with essentially straight lines having a slope of -1 . The two dashed lines indicate that the fading carrier may consist of a primary fading component with effective frequency components whose 3-db bandwidth is approximately 2.6 cps,⁷ and an additional component with approximately a 21-cps bandwidth. There is always the possibility in observations of this type that the transition may have been caused by a small amount of high-frequency components contributed by the thermal noise in the 760-cps band-pass of the receiver. In view of this, it would appear more desirable in the future to obtain carrier fade data directly in terms of the percentage of time the carrier envelope fades to and remains below a given level for specified time durations as shown later in Fig. 19 and also in terms of the effective frequency spectrum.

NOISE CHARACTERISTICS

Recent studies and measurements of the statistical characteristics of atmospheric radio noise by Hoff and Sullivan,⁸ Horner,^{9,10} Hoff and Johnson,¹¹ Yuhara, Ishida, and Higashimura,¹² and Watt and Maxwell^{6,13} combined with studies of thermal noise by Landon,¹⁴ Rice,¹⁵⁻¹⁷ Norton¹⁸ and other workers in both fields, have

⁷ Frequency spectrum analysis by H. Janes on records similar to Fig. 2 yielded 3-db response bandwidths in the order of 2 to 5 cps.
⁸ R. S. Hoff and A. W. Sullivan, "A survey of the atmospheric noise problem," *Proc. URSI X Gen. Assembly*, vol. 8, pt. 2, pp. 297-302; September, 1950.
⁹ F. Horner, "Notes on the significant characteristics of atmospheric noise," *Proc. URSI XI Gen. Assembly*, vol. 10, pt. 4, p. 32; September, 1954.
¹⁰ F. Horner and J. Harwood, "An investigation of atmospheric radio noise at very low frequencies," *Proc. IEE*, vol. 103, pt. B, pp. 743-751; November, 1956.
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¹³ A. D. Watt and E. L. Maxwell, "Characteristics of atmospheric noise from 1 to 100 kc," *Proc. IRE*, vol. 45, pp. 787-794; June, 1957.
¹⁴ V. D. Landon, "The distribution of amplitude with time in fluctuation noise," *Proc. IRE*, vol. 30, pp. 425-429; September, 1942.
¹⁵ S. O. Rice, "Filtered thermal noise, fluctuation of energy as a function of interval length," *J. Acoust. Soc. Amer.*, vol. 14, pp. 216-227; April, 1943.
¹⁶ S. O. Rice, "Mathematical analysis of random noise," *Bell Sys. Tech. J.*, vol. 23, pp. 282-332, July, 1944, and vol. 24, pp. 46-156; January, 1945.
¹⁷ S. O. Rice, "Statistical properties of a sine wave plus random noise," *Bell Sys. Tech. J.*, vol. 27, pp. 109-157; January, 1948.
¹⁸ K. A. Norton, L. E. Vogler, W. V. Mansfield, and P. J. Short, "The probability distribution of the amplitude of a constant vector plus a Rayleigh distributed vector," *Proc. IRE*, vol. 43, pp. 1354-1361; October, 1955.

TABLE I
COMMUNICATION SYSTEM PERFORMANCE COMPARISON

Fig.	System	wpm	Noise		Carrier	C/N ₁ kc			SPF‡		
			Dynamic Range			rms Carrier to rms Noise in a 1-kc Band (db) †					
			Type	db*		-10%	1%	0.1%	10%	1%	0.1%
6	A CW good operator	15	T	21	S	-1	1	(4)	12.8	10.8	7.8
7	B CW good operator	12	A	68	S	-11.5	-2	(4)	22.3	12.8	6.8
7	C CW fair operator	12	A	68	S	-3	—	—	13.8	—	—
8	D CW good operator	12	A	69	S	-10	(-2)	—	20.8	12.8	—
8	E CW good operator	16	A	69	S	-8	(0)	—	20	12	—
8	F CW good operator	20	A	69	S	-6	(1)	—	19	12	—
9	G FSK ± 17 cps	40	T	21	S	-2.3	0	1.6	18.3	16	14.4
9	H FSK ± 50 cps	60	T	21	S	0	2	3	17.8	15.8	14.8
10	I FSK ± 25 cps	60	A	68	S	0	10	17	17.8	7.8	0.8
11	J FSK ± 50 cps	60	A	69	S	3	11	15	14.8	6.8	2.8
12	K FSK ± 425 cps	60	A	50	S	10	18	21	7.8	-0.2	-3.2
13	L FSK ± 425 cps	60	A	40	ionospheric fading	12	25	34	5.8	-7.2	-16.2
14	M FM-FSK 576 TTY channels	60/ch	T	21	tropospheric fading	43	48	53	2.4	-2.6	-7.6
14	N FM 36 voice channels	100/ch	T	21	tropospheric fading	[49]	[80]		[-13.4]	[-44.4]	

* 0.001 to 90 per cent in a 1-kc band.

† For system performance as indicated. TTY and CW: character errors; voice: word errors. 1-kc effective noise band.

‡ System Performance Factor = $10 \log (\text{wpm}) - C/N_{1\text{ kc}}$.

() Extrapolated or based upon extrapolated data.

§ Based upon random word errors. Note 10 per cent word errors \approx 2 per cent character errors and 1 per cent word errors \approx 0.2 per cent character errors.

placed us in a position where we can analyze with considerable detail the interfering effects of noise.

A recent paper by Crichtow¹⁰ shows how the predictions of world-wide noise levels are being expanded to include detailed information about the character of noise to be expected at various locations, so that its interfering effect can be predicted with greater accuracy than has been possible in the past.

The cumulative envelope amplitude distributions of the noise, which are included as a basis for comparing the performance of the various radio systems in the next section, were obtained as described earlier.⁴ Since the manner in which the observed amplitude distributions vary with the bandwidth of the receiving circuit is important in interpreting system performance, Fig. 5, opposite, is included to show typical atmospheric noise characteristics.

In general, the dynamic range of the noise becomes smaller and the level is reduced as the bandwidth is reduced. The actual rms value is directly proportional to the square root of the bandwidth.⁴ This relation is true for all types of noise and bandwidths where the input frequency spectra are flat over the regions of interest. It also should be pointed out that the dynamic range only reduces to that of thermal noise and once this point is reached where the envelope distribution becomes Rayleigh, any further reductions in bandwidth only result in a change of level and not shape.¹⁴

In view of these changes in shape and level with bandwidth, and the knowledge that postdetection filtering

produces an additional change in the distribution, we do not expect our system performance or error curves to exactly follow a particular noise amplitude distribution curve. However, we can anticipate a systematic and reproducible departure which can be used as a basis for future performance prediction.

In addition to the amplitude distributions, we find it necessary to have some knowledge of the statistics of the pulse spacing of the noise envelope. Information of this type is presented in an earlier paper⁴ for a large number of times and at several locations. In general, the results indicate a noticeable departure from purely random pulse spacing for noise outside the tropics; however, since the general shape of the curves is quite similar for most of the observations, it is expected that for many systems the amplitude distribution will furnish the information necessary for prediction of system errors.

EXPERIMENTAL RESULTS

The performance of three frequently used types of radio systems—aural Morse code, frequency shift keying teletype, and voice—has been examined under various combinations of typical carrier and noise conditions.

A comparison of the performance of the various systems is given in Table I where the systems considered are divided into three primary groups—CW, frequency shift keying, and voice. These primary types of systems are next grouped into those operating against thermal noise or atmospheric noise as well as those operating with steady carriers or fading carriers. The factor $C/N_{1\text{ kc}}$ is defined as the rms carrier into the receiver, to rms noise in a 1-kc effective power bandwidth expressed

¹⁰ W. Q. Crichtow, "Noise investigation at VLF by the National Bureau of Standards," *Proc. IRE*, vol. 45, pp. 778-782; June, 1957.

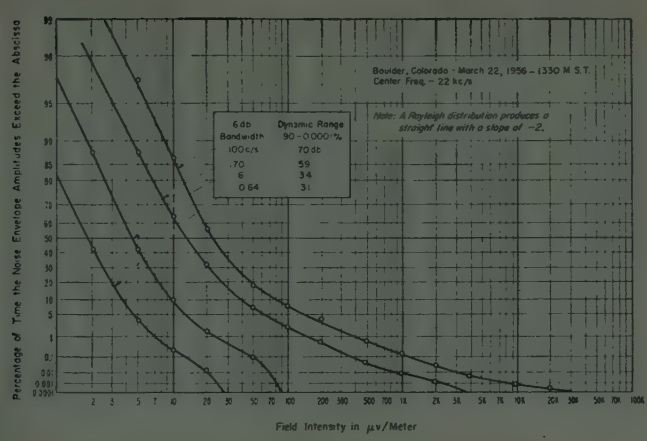


Fig. 5—Measured amplitude distributions of atmospheric noise envelopes.

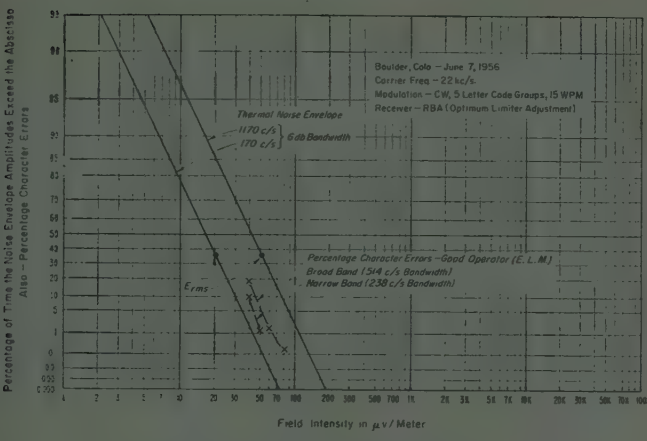


Fig. 6—Communication system performance in the presence of thermal noise.

in db.²⁰ In this paper lower case ratios are employed for voltage ratios and upper case for these ratios given in decibels. C/N_{1kc} is obtained readily from the data shown by observing that $C/N_{1kc} = C/N_b + 10 \log(y/1000)$, where y is the effective power bandwidth in which the noise is observed. Specifically, $y = 1170 \times 0.82$ and $10 \log(y/1000) = -0.2$ db. The system performance factor (SPF) is defined as $10 \log_{10} (\text{words per minute}) - C/N_{1kc}$ at the error percentages indicated which are 10 per cent, 1 per cent, and 0.1 per cent.

CW Aural Systems—Steady Carriers

The CW transmissions all consisted of five letter code groups. When comparing the SPF for systems A and B, Figs. 6 and 7, it is observed that at 10 per cent errors a good operator can perform more efficiently in the pres-

²⁰ It should be noted that c/n_{1kc} is based upon the rms noise in a 1-kc effective power band rather than upon the rms noise in the receiver IF filter. The usual C/N based on the carrier and noise out of the receiver bandwidth can be obtained readily since the rms value of noise is directly related to the square root of bandwidth, and the carrier attenuation also can be obtained. It should be mentioned that in our noise measuring equipment the ratio of 3-db to 6-db bandwidths is 0.60 for the 170-cps narrow band and 0.64 for the 1170-cps wide band. The effective noise power bandwidth is approximately 0.82 times the 6-db bandwidth in both cases.

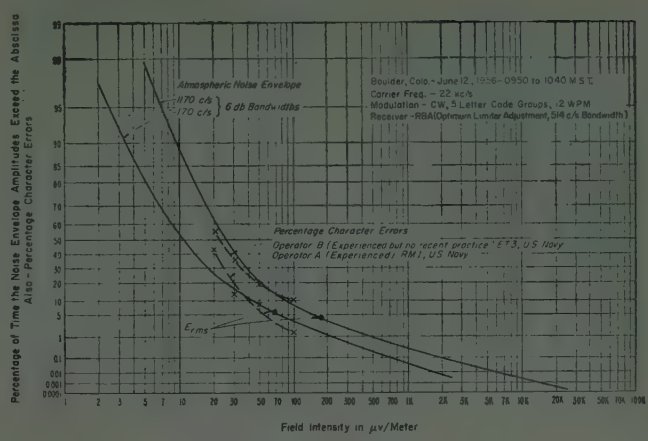


Fig. 7—Communication system performance in the presence of atmospheric noise.

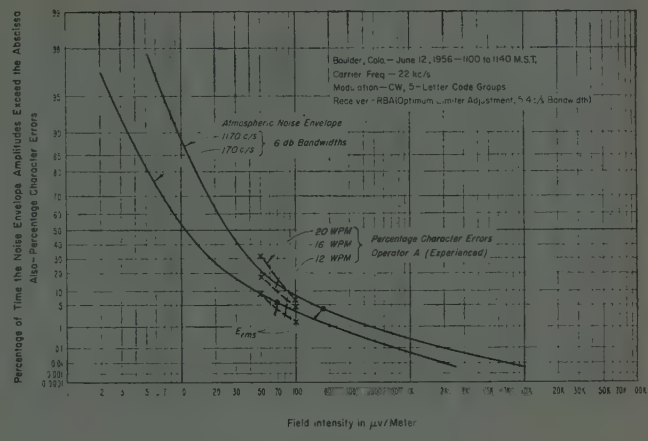


Fig. 8—Communication system performance in the presence of atmospheric noise.

ence of atmospheric noise while at 0.1 per cent errors his efficiency is greater with thermal noise.

From systems B and C it is evident that the level of performance obtained under typical VLF atmospheric noise conditions is very dependent upon the skill of the individual operator; however, it also has been found that under similar noise conditions the level of performance for skilled operators exhibited a much smaller spread than anticipated.

Fig. 8, systems, D, E, and F, shows the effect of varying the rate of information transmission with the same skilled operator. In general, a reduction of keying rate for a fixed carrier level results in a reduction of errors. This effect is not expected to be linear over all keying rates since the human ear has a limited effective integration length.²¹ It is interesting to note that the SPF change is rather small for the keying rates considered. Before passing to the automatic systems, it should be mentioned that, in our experience, human operators find it very difficult to perform at character error rates of 0.1 per cent or less.

²¹ W. R. Garner, "Auditory thresholds of short tones as a function of repetition rates," *J. Acoust. Soc. Amer.*, vol. 19, pp. 600-608; July, 1947.

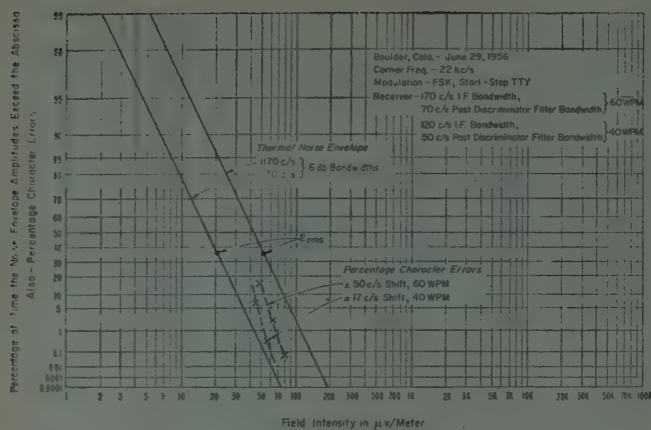


Fig. 9—Communication system performance in the presence of thermal noise.

FSK Systems—Steady Carrier

Frequency shift keying systems G and H, Fig. 9, illustrate operation under thermal noise and steady carrier conditions. These 60-wpm start-stop teletype systems were operated with a shift of ± 50 cps, a receiver 6-db IF bandwidth of 170 cps, and a postdiscriminator filter with a 70-cps 6-db cutoff. The 40-wpm system was operated with a shift of ± 17 cps, a receiver 6-db IF bandwidth of 120 cps, and a postdiscriminator filter with a 50-cps 6-db cutoff. As would be expected, the 40-wpm system operated at a lower carrier level for equivalent performance than was required by the 60-wpm system. In addition, it should be noted that the slope of the error curves is greater than that of the noise envelope. This is typical of FSK systems and is caused by the ability of FSK receivers to reject high amplitude impulses because of limiting and postdiscriminator filtering.

Fig. 10 shows the performance of a 60-wpm teletype system employing ± 25 cps shift in the presence of atmospheric noise. It can be noted that the radio system error curve lies considerably to the right of the atmospheric noise envelope curves rather than between them as was true in the thermal noise case. Fig. 11 illustrates the performance of a similar system except that ± 50 cps shift is employed. The character error curve now is considerably steeper than was the case in Fig. 10. In addition, it can be noticed that the high error portion of the error curve lies further to the right of the noise envelope curves than was true in Fig. 9, while at the low error rates the error curve lies between the two noise envelope curves. This difference in performance characteristics is typical of FM or FSK systems as the frequency deviation is increased.^{22,23}

When the SPF of systems A and G (thermal noise) are compared at 0.1 per cent errors, the frequency shift

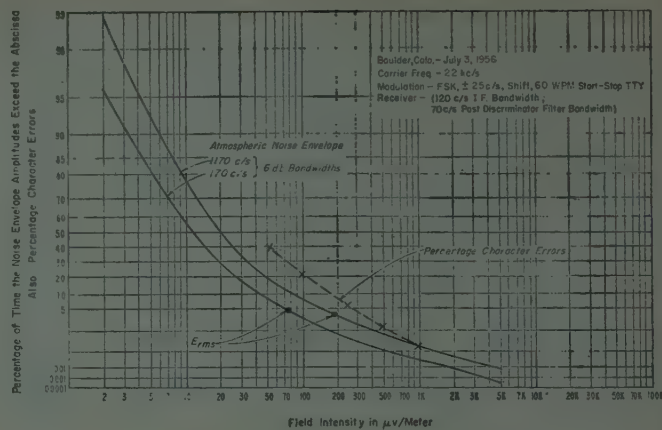


Fig. 10—Communication system performance in the presence of atmospheric noise.

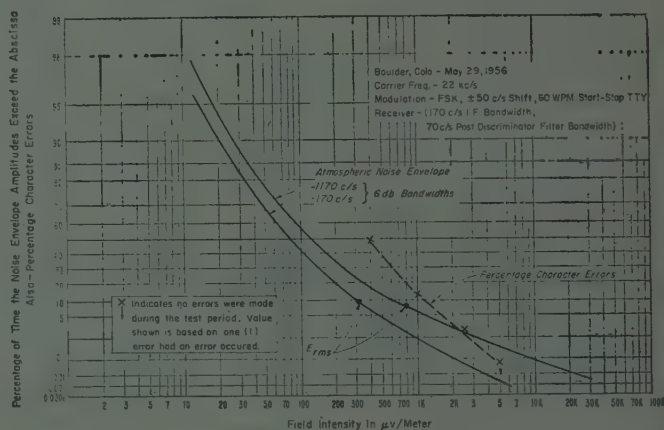


Fig. 11—Communication system performance in the presence of atmospheric noise.

automatic teletype systems performance is seen to be 6.6 db higher than was possible for even the best CW operator. This results from at least two factors. First, the CW Morse code is basically less efficient than the teletype code, and second, the human operator suffers from fatigue under long periods of operation and is unable to perform well at very low error rates.

An interesting fact which can be observed is that it is essential to know the maximum allowable errors for a given communication circuit if an optimum choice of system factors is to be made. As an example, we can compare the relative performance of the frequency shift teletype systems I and J employing ± 25 cps shift and ± 50 cps shift. For these two systems it is noted that the ± 25 -cps shift system has the higher SPF at 10 to 1 per cent error rates. On the other hand, if a very high quality system is required, such as 0.1 per cent errors or less, it is readily apparent that the SPF is greater now for the ± 50 -cps shift system. If we still further increase our frequency shift to ± 425 cps, Fig. 12, a shift frequently employed on high-frequency radio teletype circuits, it is observed that the SPF is considerably lower at all error rates with the greatest difference at the 10 per cent values.

²² M. G. Crosby, "Frequency modulation noise characteristics," *Proc. IRE*, vol. 25, pp. 472-514; April, 1937.

²³ A. D. Watt, "Statistical Characteristics of Sampled and Integrated A-M and F-M Noise," Naval Res. Lab., Washington, D. C., Rep. No. 3856; October 22, 1951.

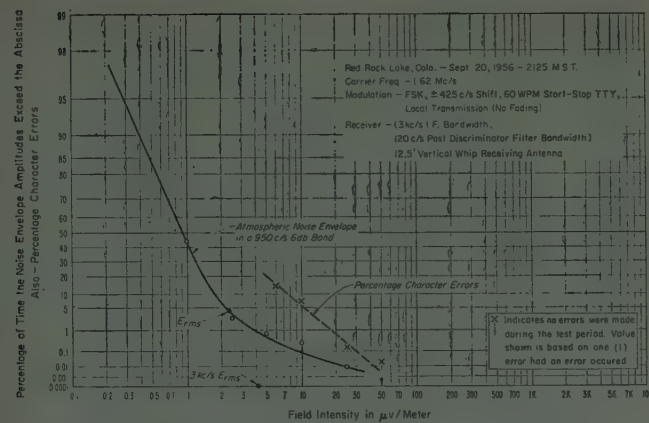


Fig. 12—Communication system performance in the presence of atmospheric noise.

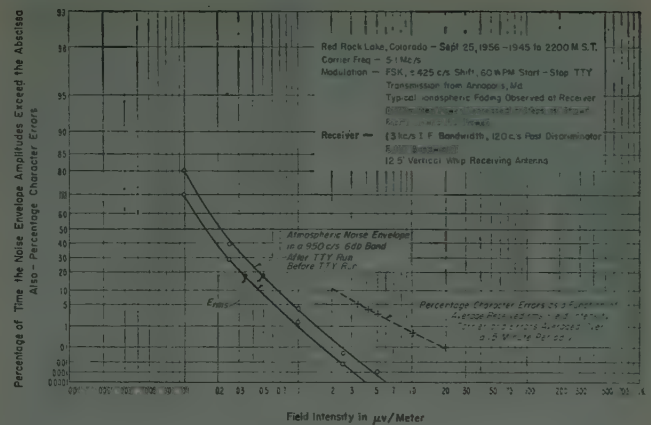


Fig. 13—Communication system performance in the presence of atmospheric noise.

FSK and FM Systems—Fading Carrier

When a fading carrier is employed, it is seen that the SPF is reduced considerably at all error rates with the greatest reduction occurring in the low percentage error region.

Fig. 13, system L, shows a typical frequency shift teletype transmission employing a 5.1-mc carrier with normal ionospheric fading. Each of the data points shown corresponds to a message approximately 15 minutes in length and the field intensity indicated is the average field intensity for each of these periods. The low error points are seen to be considerably to the right of the noise envelope curve. In practice, diversity systems are frequently employed to recover some of the carrier efficiency.

When systems K and L are compared, the SPF at 0.1 per cent errors is found to be reduced by 14 db. It should be noted also that the dynamic range of the atmospheric noise was less on the ionospheric fading, system L, than was true of the steady carrier, system K. Had the atmospheric noise dynamic ranges been the same, it is very likely that the SPF would have been reduced by an even greater amount.

System M, Fig. 14, employed a carrier frequency of 581 mc on a beyond-the-horizon path. The receiver noise in the 4.5-mc, 6-db, 3.7-mc effective IF band was the limiting factor so far as the production of errors was concerned. The basic transmitter was frequency modulated and employed 36 normal voice channels with a modulation index of 1 as subcarriers on the main carrier. Each of these voice channels could be subdivided into 16 frequency shift teletype channels although only 3 subcarrier units were available on the channel employed, which was No. 24 with a center frequency of 60 kc. The transmitter modulator gain was set so that an input sine wave of -1.4 dbm yielded ± 60 -kc shift, *i.e.*, $m=1$. During the voice tests the level was set at the recommended level of -13 dbm which is 11.6 db below the maximum allowable swing per channel or ± 15.8 kc. For the 60-wpm start-stop teletype tests, an audio subcarrier employing a shift of ± 35 cps was set at the

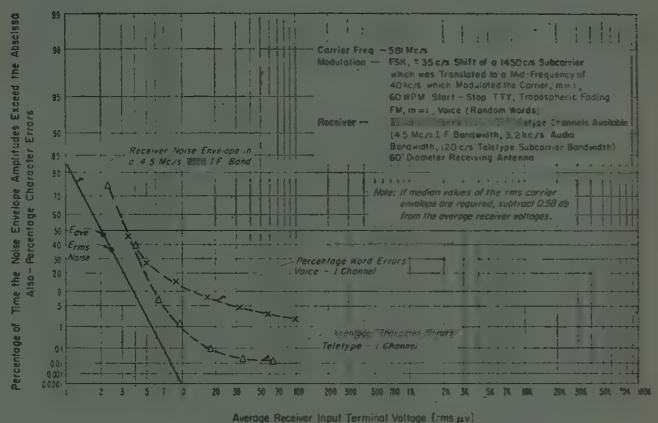


Fig. 14—Forward scatter tropospheric propagation circuit performance tests.

recommended level of -29 dbm which yielded a carrier swing of ± 2.5 kc. Since the subcarrier receiving equipment employed a low-pass filter with an estimated (6-db) cutoff of 50 cps and a 120-cps (6-db), 100-cps (3-db) bandwidth IF filter, the teletype channels could be spaced every 200 cps. In the 200 to 3400-cps voice band available, this would permit 16 teletype circuits, and it would appear that even if all 16 channels were operating, a level of -25.6 dbm could have been employed without exceeding the allotted swing per primary channel. If this level had been employed, it is expected that slightly improved performance would have resulted. In order to obtain the system performance curves, an attenuator was inserted in the antenna circuit and the average received voltage was reduced as shown. For the voice performance curves, random words were read slowly and distinctly while the operator at the receiving end recorded what he thought he had heard. The speaking rate was in the order of 100 words per minute although the pauses between words to permit writing reduced the actual rate to 15 words per minute. For the teletype performance curves, character errors were counted from a standard "quick brown fox" message.

Since it was possible to employ up to 16 different tele-

type channels for each voice channel, a total of 576 teletype channels were available in this system. Here is a practical case where a fading carrier was operating in the presence of thermal noise. The teletype SPF at the 10 per cent error rate is found to be 15.4 db below the single channel 60-wpm teletype systems operating under thermal noise conditions and steady carrier, and at the 0.1 per cent error level the performance is 23.4 db lower.

System N, employing frequency modulation with a voice signal, is shown on the last line of Table I. The existing carrier and noise conditions were the same as for the preceding teletype example. When voice signals are used, it is found that the SPF decreases very markedly. It should be emphasized that these SPF's are based on word errors for the voice communication system and that they would actually correspond to approximately 2 per cent and 0.2 per cent character errors. However, this still results in a considerably lower performance factor for the voice communication system.

COMPARISON WITH THE EXPERIMENTAL RESULTS OF OTHERS

It may be of interest to compare our results with those obtained by others for automatic teletype systems operating in the presence of thermal noise. Fig. 15 shows the thermal noise envelope in a 1-kc band, which is used as a reference for all the system performance curves indicated. Two sets of data, the dots adapted from Jordan, *et al.*,²⁴ and the triangles adapted from Doelz,²⁵ were used to plot the ± 425 -cps shift start-stop curve. The curve lying just to the left of the noise envelope is for a start-stop system employing ± 50 -cps shift and is the data from Fig. 9. The curve with the square data points was adapted from Jordan²⁴ and indicates the experimental performance of a multiple frequency shift system. This particular system employed seven different possible frequency levels spaced by approximately 80 cps per frequency interval. Actually, only six frequencies were employed in transmitting information while the seventh was used for synchronizing purposes. It can be seen that this system is more efficient than the optimally designed ± 50 -cps binary FSK start-stop system. In addition, the curve on the left has been included with the circular experimental data points adapted from Doelz,²⁵ which indicated the performance of his predicted wave radio teleprinter system.

COMPARISON OF EXPERIMENTAL RESULTS WITH THEORETICAL CALCULATIONS OF ERRORS

When the many factors involved in accurately calculating expected errors for typical systems are considered, it soon becomes apparent that a detailed analysis of all the systems described in this paper is beyond the scope of our present analysis.

²⁴ D. B. Jordan, H. Greenberg, E. E. Eldredge, and W. Serniuk, "Multiple frequency shift teletype systems," *Proc. IRE*, vol. 43, pp. 1647-1655; November, 1955.

²⁵ M. L. Doelz, "Predicted-wave radio teleprinter," *Electronics*, vol. 27, pp. 166-169; December, 1954.

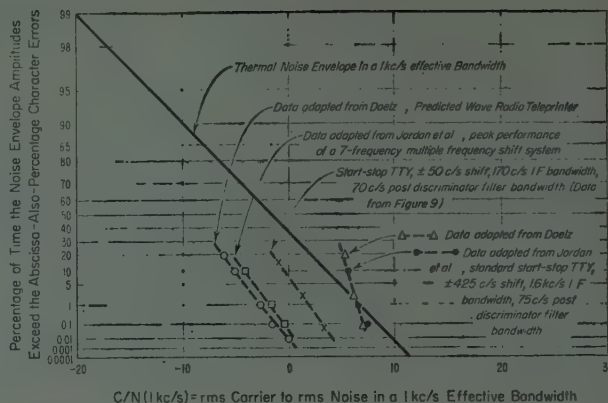


Fig. 15—Comparison of performance in thermal noise of 60-wpm teletype systems.

Montgomery²⁶ has shown that the errors in a binary narrow-band frequency modulation system can be considered as being one half the probability of the noise envelope exceeding the carrier envelope. The basis for this error calculation was pointed out by Corrington²⁷ when he showed that the average frequency of two components in a given circuit is exactly equal to that of the stronger of the two frequency components. When a sequential communication system such as the standard five-unit teletype is considered, the probability of teletype symbol error is readily obtained by the expression $P_e = 1 - (1 - p)^5$ when each of the binary elements is independent and has a probability of error p . The actual relationship between the errors in a practical start-stop system will depend to some extent upon the characteristics of the circuits in the receiving equipment as well as those of the start-stop teletype equipment. In general, assuming a teletype system where the probability of a binary error in a given element is largely independent of other elements (since the teletype employed in these tests had automatic line feed and carriage return), the probability of obtaining a correct character in a start-stop system can be estimated by

$$P_e \approx (1 - p)^5 [(1 - p)^2]^6 = (1 - p)^{17} \quad (1)$$

where p is the probability of an error in each binary element. The first term $(1 - p)^5$ is the probability of having the five information carrying elements correct. The next term $(1 - p)^2$ results since the preceding character's stop element and the start element of the particular character under consideration must also be correct. Once the receiving teletype loses synchronism with the transmitter there will be a series of errors whose length, based on observation, will average approximately six characters. We then can assume that for our given character to be correct, we must have, on the average, the pre-

²⁶ G. F. Montgomery, "A comparison of amplitude and angle modulation for narrow-band communication of binary-coded messages in fluctuation noise," *Proc. IRE*, vol. 42, pp. 447-454; February, 1954.

²⁷ M. S. Corrington, "Frequency modulation distortion caused by common- and adjacent-channel interference," *RCA Rev.*, vol. 7, pp. 522-560; December, 1946.

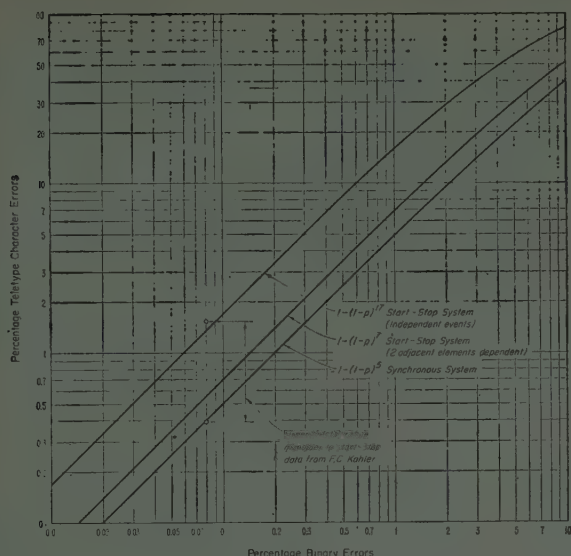


Fig. 16—Teletype character errors expected for various binary signal element errors.

ceding six characters' start and stop elements correct, and for this reason the last expression is raised to the sixth power. The time out of synchronism can vary with printers, and it is possible that in some cases four or five characters could be employed. Eq. (1) is a rough approximation since there are numerous combinations for obtaining a correct character; however, it is expected to be sufficiently accurate for most applications.

In view of the preceding considerations, it is evident that the probability of a given start-stop character being in error is

$$P_e \approx 1 - (1 - p)^{17} \approx 17p \text{ for small values of } p. \quad (2)$$

This particular start-stop teletype character error is plotted as a function of binary errors in Fig. 16. Also plotted are the character errors to be expected from a synchronous five-element system.

It is interesting to note that experimental comparisons by Kahler²⁸ of character errors in start-stop and synchronous systems in the 1 per cent character error range yield a difference in errors very close to that predicted (2).

When the errors in a given binary element are not independent, such as may be caused by fading or noise variations which are correlated over at least two binary elements, the resulting character errors are considerably less than when the errors are independent. If it is assumed that two adjacent elements are dependent, the expected teletype character errors can be approximated by

$$P_e \approx 1 - (1 - p)^7. \quad (3)$$

²⁸ F. C. Kahler, "The Effect of Fluctuations in Signal Strength on the Relative Performance of Start-Stop and Synchronous Teletype Systems," Naval Res. Lab., Washington, D. C., Rep. No. 4554; August 5, 1955.

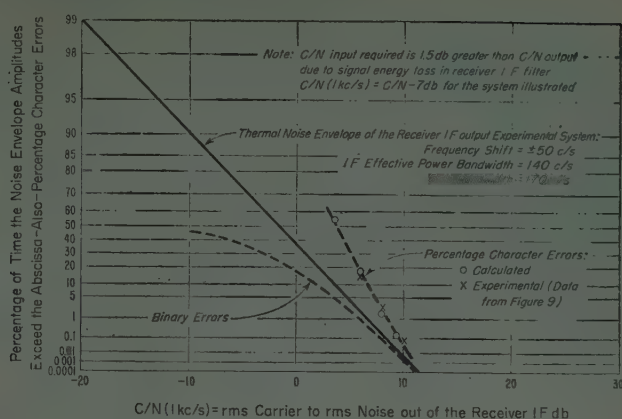


Fig. 17—Comparison of calculated and experimental FSK teletype system performance in the presence of thermal noise.

Now we are in a position to calculate the start-stop system errors expected, and system H, which has a steady carrier and thermal noise, shall be considered first. Fig. 17 plots the expected thermal noise envelope in the 140-cps effective IF band. The binary error curve is obtained by simply dividing the envelope probability values by 2. From this binary error curve, we now apply the corrections obtained from Fig. 16 for the five-unit synchronous system error curve and start-stop curve. It should be noted that the experimental errors have been plotted 1.5 db lower than would be expected from a simple bandwidth conversion from Fig. 9. This allows for the 1.5-db loss in carrier power in the receiver IF due to the ± 50 -cps frequency shift. When converting to receiver input requirements relative to a 1-kc effective noise band, we must use the relation $C/N_{1kc} = C/N + \text{db loss due to shift} + 10 \log(y/1000)$ where y is the receiver IF effective power bandwidth.

An attempt is made now to calculate the errors expected with a steady carrier and typical atmospheric noise as would be found in the VLF region. Fig. 18 plots the atmospheric noise envelope that would be expected in a 120-cps band. This curve has been reconstructed based on a method described by Fulton.²⁹ The binary error curve is obtained again by dividing the noise envelope probability by 2, and the start-stop errors are obtained with the aid of Fig. 16. The experimental points are plotted directly from Fig. 10 since the shift in this case reduces the carrier out of the IF by less than 0.2 db. Before going on to the next example, it should be noted that in system J (Fig. 11), where a shift of ± 50 cps is employed, the resulting errors cannot be calculated in the manner that they were for system I of Fig. 10.

The last system to be considered is that represented by system M, which has a tropospheric forward scatter carrier in the presence of thermal noise. As pointed out

²⁹ F. F. Fulton, Jr., "The effect of receiver bandwidth on amplitude distribution of VLF atmospheric noise," *Symp. Propagation of VLF Radio Waves*, Boulder, Colo., vol. 3, pp. 37-1 to 37-19; January 23-25, 1957.

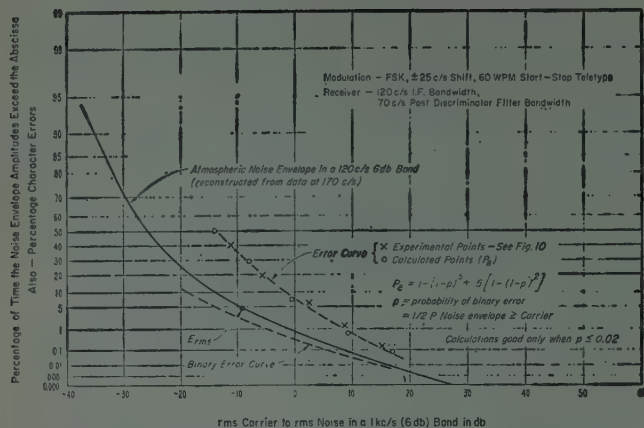


Fig. 18—Comparison of calculated and experimentally determined errors.

by Montgomery,^{26,30} the binary error rate can be calculated as one half the per cent of time that the carrier envelope is less than or equal to the noise envelope, provided the carrier envelope and the noise envelope amplitude distributions are not modified in shape or position by postdetection or signal selection filtering. It is rather evident from the description of system M that it does not meet these criteria. It can be seen from Fig. 19 that assuming a sampling period τ , which is short compared with the reciprocal of the carrier energy spectrum, the carrier envelope voltage is Rayleigh distributed as expected. When τ is increased, the distribution departs from Rayleigh, as shown.

For slowly fading carriers and narrow-band systems such as the single sideband system described by Morrow, *et al.*,³¹ we could expect to calculate binary errors from the cumulative distribution of the percentage of time that the instantaneous noise envelope exceeds the carrier envelope. For Rayleigh distributions this is

$$P\left(\frac{n}{c} \geq 1\right) = \frac{1}{1 + (C/N)^2} \quad (4)$$

where C and N are the rms values of the carrier and noise.

Since the curves of Fig. 19 are expected to vary from the Rayleigh distribution with time and the various propagation path parameters, it may be necessary to obtain the cumulative distribution of the per cent of time that the carrier fades to and remains below the noise envelope for at least τ seconds by a method described by Huntington,³² which can be done graphically if desired.

For the wide-band FM-FSK system M, the method attempted for calculating errors is to first estimate per-

³⁰ G. F. Montgomery, "Message error in diversity frequency-shift reception," *Proc. IRE*, vol. 42, pp. 1184-1187; July, 1954.

³¹ W. E. Morrow, Jr., C. L. Mack, Jr., B. E. Nichols, and J. Leonard, "Single-sideband techniques in UHF long-range communications," *Proc. IRE*, vol. 44, pp. 1854-1873; December, 1956.

³² E. V. Huntington, "Frequency distribution of product and quotient," *Ann. Math. Stat.*, vol. 10, no. 2, pp. 195-198; June, 1939.

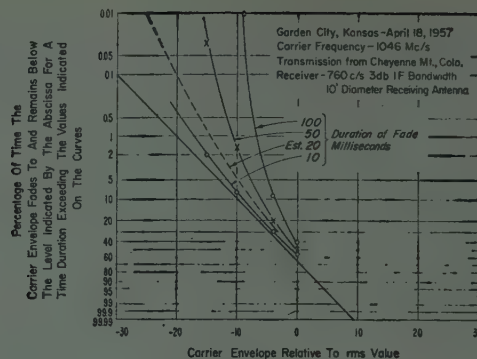


Fig. 19—Tropospheric scatter carrier fade length characteristics.

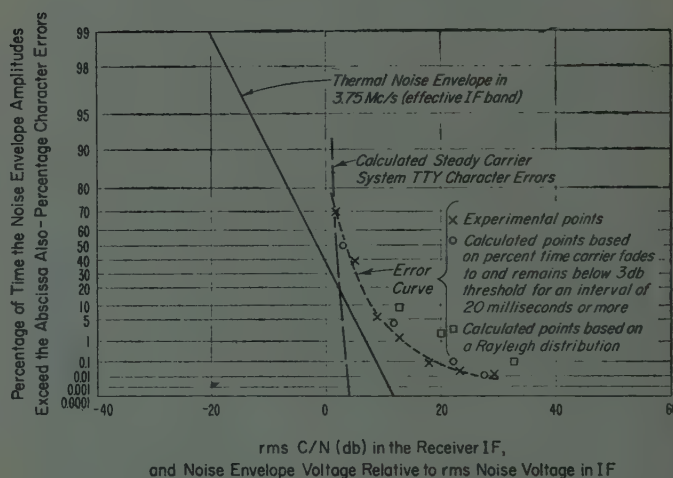


Fig. 20—Comparison of calculated and experimentally determined errors for FM, FSK forward scatter link, start-stop 60-wpm teletype system M.

formance under steady carrier conditions. This is done by calculating the FM noise improvement which can be shown from Stumpers³³ to be

$$\frac{C/N \text{ (subcarrier)}}{C/N \text{ (first IF)}} \sim \frac{\Delta f}{f} \times \sqrt{\frac{B_{if}}{2B_{sc}}} \quad (5)$$

where Δf is the subcarrier shift, f is the subcarrier frequency, B_{if} is the first IF bandwidth, and B_{sc} is the subcarrier IF bandwidth. For system M this is a gain of 15 db. The gain in the subcarrier FSK system is^{23,33}

$$\frac{C/N \text{ (to keying circuit)}}{C/N \text{ (subcarrier)}} \sim \frac{f_D \sqrt{3B_{sc}}}{f_A^{3/2}} \quad (6)$$

where f_D is one half the total audio subcarrier frequency shift, and f_A is the cutoff frequency of the low-pass filter following the discriminator. For system M this is a gain of 5.4 db. The total gain of about 20 db is valid only when the input $C/N \geq 10$ db. It can be shown using this FM noise improvement and the threshold effect at $C/N \leq 6$ db, that our teletype character error curve must lie very close to the dashed curve in Fig. 20. The actual

³³ F. L. H. M. Stumpers, "Theory of frequency-modulation noise," *Proc. IRE*, vol. 36, pp. 1081-1092; September, 1948.

errors with a fading carrier should not be obtained by combining the distributions of this dashed curve and the appropriate carrier fade characteristic. Since the system steady-state character error curve in Fig. 20 is approximately a vertical line at $C/N=3$ db in Fig. 17, we can assume this and directly obtain an estimate of teletype character errors from Fig. 19. If the Rayleigh curve is used, the squares are obtained which do not agree very well with the observed errors. While, if it is assumed that to be certain of a teletype character error the carrier must fade to and remain below $C/N=3$ db for at least 20 msec (a binary element length), the circles are obtained.

Although the agreement appears to be good, caution should be exercised in using this type of calculation until further comparisons can be made with experimental results where the actual path statistics can be employed.

APPLICATION OF RESULTS TO CALCULATION OF REQUIRED TRANSMITTER POWER

A relatively simple expression described by Norton^{34,35} for calculating the transmitter power required for a specified grade of service on a given radio transmission path can be written

$$P_t = L_t + L_{bm} - G_p + C/N_{1\text{kc}} + F_m + T_z - 174 \text{ db.} \quad (7)$$

Each of the terms in (7) is expressed in decibels: P_t is the transmitter power in decibels above 1 watt; L_t is the loss in the transmitting antenna circuit and the transmitting antenna transmission line; L_{bm} is the median value of basic transmission loss; G_p is the path antenna gain; $C/N_{1\text{kc}}$ is the rms signal to rms noise in a 1-kc effective power band required for the specified grade of service (see Table I); F_m is the effective total noise figure³⁶ and includes the effects of the antenna, external noise as well as the receiver noise, together with the re-

ceiving antenna circuit and transmission line loss (it is assumed that the receiver incorporates gain adequate to ensure that the first circuit noise is detectable). When we assume a given median value of basic transmission loss L_{bm} , and median noise F_m , we can readily calculate the power required for 50 per cent of the time to yield 10, 1 and 0.1 per cent errors with the systems indicated in Table I for the types of carrier and noise shown. If it now is necessary to calculate the power required to assure this given quality of message for a given percentage x of all hours, it is necessary to include the additional factor T_z described in greater detail by Crichlow, *et al.*³⁶ which allows for expected variations in transmission loss and received noise about the above median predicted values. For uncorrelated normally distributed hourly medians of L_b and F , T_z can be found from the combined distribution, which is also a normal distribution whose deviation is equal to the root-sum-square of the individual deviations of L_b and F . The last term, -174 , is the thermal noise power in a 1-kc band in db relative to 1 watt.

It should be noted that the only factor in (7) under the control of the terminal system designer is $C/N_{1\text{kc}}$, and for a given type and rate of transmitting information $C/N_{1\text{kc}}$ provides an index for comparing similar systems.

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³⁴ K. A. Norton, "Transmission loss in radio propagation," *PROC. IRE*, vol. 41, pp. 146-152; January, 1953.

³⁵ K. A. Norton, "Point-to-point radio relaying via the scatter mode of tropospheric propagation," *IRE TRANS. ON COMMUNICATIONS SYSTEMS*, vol. CS-4, pp. 39-49; March, 1956.

³⁶ W. Q. Crichlow, D. F. Smith, R. N. Morton, and W. R. Corliss, "World-Wide Radio Noise Levels Expected in the Frequency Band from 10 Kilocycles to 100 Megacycles," *Natl. Bur. of Standards Circular 557*, August 25, 1955. Available from the Supt. of Documents, U. S. Govt. Printing Office, Washington 25, D. C., price 30 cents.

Structure-Determined Gain-Band Product of Junction Triode Transistors*

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Summary—This paper discusses some fundamental frequency limitations of the junction triode. It also describes briefly practical accomplishments with germanium diffused base transistors of the type reported by Lee. Finally, the frequency limitations of the junction triode are compared with those of the field effect transistor and the analog transistor.

For transistors of the mesa type with linear emitter and base electrodes (i.e., an emitter stripe with parallel base contact stripes a fraction of the emitter width distant on each side), the (power gain)^{1/2}(bandwidth) product is found to be about $7.5 \times 10^6/s$ cps where s is emitter stripe width in centimeters. This is an order of magnitude better than the corresponding figures for field effect and analog transistors. For operation at or below the alpha cutoff frequency, the gain-band product is shown to be nearly independent of the particular alpha cutoff frequency selected. This independence arises from the reciprocity between collector depletion layer capacitance per unit area and collector depletion layer transit time. This transit time effectively determines alpha cutoff frequency in optimum gain-band designs.

INTRODUCTION

ALL transistors made or analyzed to date have shown finite upper frequency limits for amplification or oscillation. In this paper, frequency limits of junction triode transistors are examined in terms of the dependence of (power-gain)^{1/2}(bandwidth) product K on device structure and operating biases. This gain-band figure is in principle equal to the maximum frequency of oscillation.

The gain-band theory developed is then compared with experimental results on p - n - p germanium diffused base transistors. A final section summarizes results and compares theoretical performance with that reported previously for the field effect transistor^{1,2} and the analog transistor.^{3,4}

The structure analyzed is a somewhat idealized diffused base transistor of the mesa type,⁵ as shown in Fig. 1. The width s of the emitter electrode, together with the spaces of width $s/2$ separating this electrode from the highly conducting base contacts parallel to it on both sides, will be found to be a key high frequency parameter. Thicknesses w of the base layer and x_m of the reverse biased collector depletion layer (Fig. 2) substantially determine alpha cutoff frequency.

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¹ W. Shockley, "A unipolar 'field-effect' transistor," *Proc. IRE*, vol. 40, pp. 1365-1376; November, 1952.

² G. C. Dacey and I. M. Ross, "The field effect transistor," *Bell Sys. Tech. J.*, vol. 34, p. 1149; November, 1955.

³ W. Shockley, "Transistor electronics: imperfections, unipolar and analog transistors," *Proc. IRE*, vol. 40, pp. 1289-1313; November, 1952.

⁴ W. Shockley, U. S. Patent No. 2,790,037; filed March 14, 1952, granted April 23, 1957.

⁵ C. A. Lee, "High frequency diffused base germanium transistor," *Bell Sys. Tech. J.*, vol. 35, p. 23; January, 1956.

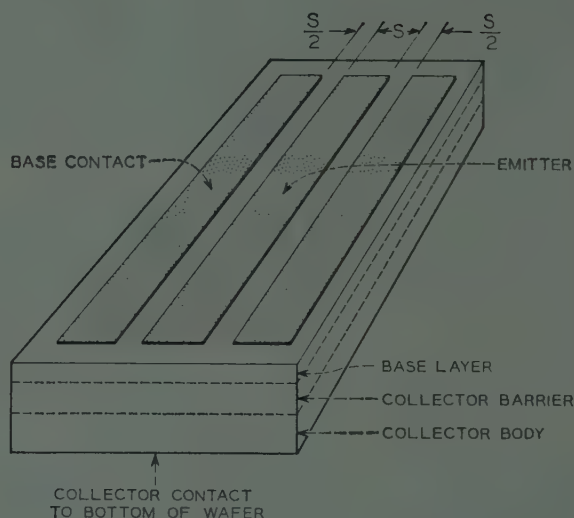


Fig. 1—Idealized transistor with linear emitter electrode and base contacts.

The analysis is simplified considerably by the assumption that collector body resistance is negligible. For this to be true, the collector contact plane at the bottom of the wafer (Fig. 1) must be close to the collector face of the collector depletion layer.

GAIN-BAND AND STRUCTURE

The frequency performance of most junction triodes is quite fully characterized by a gain-band figure of merit which includes 3 parameters.⁶ These are the alpha cutoff frequency (f_a), the ohmic base resistance (r_b'), and the collector barrier capacitance (C_c). A convenient form of the gain-band expression is:

$$K \equiv (\text{Power Gain})^{1/2}(\text{Bandwidth}) \simeq f_{\max \text{ osc}} = \frac{1}{4\pi} \left(\frac{1}{r_b' C_c \tau_{ec}} \right)^{1/2} \quad (1)$$

in which τ_{ec} is the emitter-to-collector signal delay time and is approximately $1/(2\pi f_{ab})$.

The parameters r_b' and C_c can be related to emitter stripe width s , base layer sheet resistance R_{\square} , and collector capacitance per cm² C_{ca} . Considering only the part of the transistor from the center line of the emitter

⁶ R. L. Pritchard, "Frequency response of grounded-base and grounded-emitter transistors," given at the AIEE Winter Meeting, New York, N. Y.; January, 1954. The gain-band expression:

$$(\text{Power Gain})^{1/2}(\text{Bandwidth}) = \frac{f_a}{8\pi r_b' C_c}$$

is now widely accepted for junction triodes except those of the grown junction type.

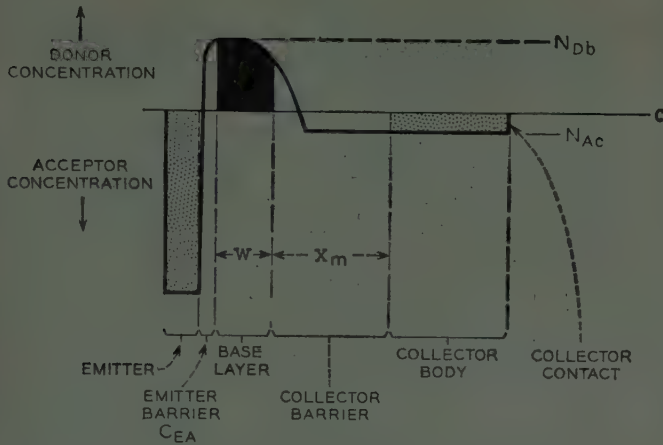


Fig. 2—Diffused base transistor—one-dimensional impurity density profile.

stripe to the near edge of one base contact,⁷ and assuming the electrode stripes are one cm long, we find:

$$C_c = sC_{ca} \quad (2)$$

$$r_b' = \frac{2sR_{\square}}{3} \quad (3)$$

In deriving (3), it was assumed that R_{\square} was the same under the emitter and between the emitter and the base contact. The result derived by Pritchard⁸ for base resistance of rectangular areas was used in the analysis.⁹

Putting (2) and (3) into (1) gives:

$$K = \frac{1}{4\pi s} \left(\frac{3}{2R_{\square}C_{ca}\tau_{ec}} \right)^{1/2} \quad (4)$$

which shows that, for fixed ratios of stripe spacing to stripe width, emitter stripe width directly determines the (power gain)^{1/2}(bandwidth) product of a junction triode. The result is not surprising, because the $r_b'C_c$ time constant of this structure varies as s^2 . The frequency response is also determined by the factor $R_{\square}C_{ca}\tau_{ec}$ which should be made as small as possible for maximum response.

THE ONE-DIMENSIONAL FACTOR $R_{\square}C_{ca}\tau_{ec}$

The factor $R_{\square}C_{ca}\tau_{ec}$ depends on applied biases and on the one-dimensional distribution of impurities between the emitter and the collector contact, such as is shown in Fig. 2. Minimum values of $R_{\square}C_{ca}\tau_{ec}$ for particular assumptions will be found by examining first the individual dependences of R_{\square} , C_{ca} , and τ_{ec} on device structure and then the joint dependence of their product.

⁷ The capacitance of the portions of the collector barrier opposite to and outside of the base contacts has substantially no resistance in series with it. Since it contributes no RF power losses, it does not affect maximum frequency of oscillation. Since it causes feedback from collector to base, it reduces the gain-band product for base band applications. The effect on bandwidth is of the order $\sqrt{2}$ and is neglected here.

⁸ R. L. Pritchard, "Advances in the understanding of the $p-n$ junction triode," *Proc. IRE*, vol. 46, pp. 1130-1141; June, 1958.

⁹ The approximation for r_b' in (3) is reasonable when most of the base resistance is contributed by the portion between emitter edge and base contact stripe. Eqs. (3) and (1) are greatly modified when this contribution is negligible (see footnote 8).

Collector capacitance per cm^2 (C_{ca}) is simply the parallel plate capacitance of the collector depletion layer:

$$C_{ca} = \frac{\epsilon}{x_m} \quad (5)$$

where ϵ is the dielectric constant of the semiconductor and x_m is the depletion layer thickness (Fig. 2).

The principal components of the emitter-collector delay time (τ_{ec}) are the emitter charging time

$$\left(\frac{kT}{qJ_E} C_{EA} \right),$$

the base transit time (w^2/nD_{pb}), and the collector depletion layer drift delay time ($x_m/2v_{sc\text{lim}}$):

$$\tau_{ec} = \left(\frac{kT}{qJ_E} C_{ca} + \frac{w^2}{nD_{pb}} + \frac{x_m}{2v_{sc\text{lim}}} \right). \quad (6)$$

In (6), J_E is dc emitter current density, C_{ca} is emitter barrier capacitance per cm^2 , n is a constant between 1 and 6 depending on the form of the base layer impurity distribution,¹⁰⁻¹² D_{pb} is minority carrier diffusion constant in the base layer, $v_{sc\text{lim}}$ is the lattice-scattering-limited maximum drift velocity for carriers passing through the reverse biased collector barrier region, and w and x_m are given in Fig. 2. For minimum τ_{ec} , J_E should be as large as possible. However, the maximum current which can reasonably be carried through the collector body is:¹³

$$J_{\text{max}} = qv_{sc\text{lim}}N_{Ac} \quad (7)$$

where N_{Ac} is collector body impurity concentration (Fig. 2). N_{Ac} also affects x_m because collector-to-base breakdown voltage (BV_{CB}) decreases as N_{Ac} increases.¹⁴ Collector depletion layer thickness at breakdown also decreases with increase of N_{Ac} .¹⁵

C_{ca} varies as $N_{Db}^{1/2}$ and also increases somewhat as J_E increases because of the reduction in emitter barrier potential needed to pass larger current densities. These trends suggest that, for fixed x_m and fixed impurity density per unit area of base layer, there is a definite minimum in τ_{ec} .

¹⁰ H. Krömer, "Zur theorie des Diffusions und des driftransistors," Parts I-III, *Arch. elektr. Übertr.*, vol. 8, pp. 223-228; May, 1954; pp. 363-369; August, 1954; pp. 499-504; November, 1954.

¹¹ "Der driftransistor," *Naturwiss.*, vol. 40, pp. 578-579; November, 1953.

¹² "The drift transistor," in "Transistors I," RCA Labs., Princeton, N. J., pp. 202-220; 1956.

¹³ J. L. Moll and I. M. Ross, "The dependence of transistor parameters on the distribution of base layer resistivity," *Proc. IRE*, vol. 44, pp. 72-78; January, 1956.

¹⁴ L. J. Varnerin, "Stored charge method of base transit analysis," to be submitted to the IRE.

¹⁵ E. J. Ryder, "Mobilities of holes and electrons in high electric fields," *Phys. Rev.*, vol. 90, p. 766; June, 1953.

¹⁶ S. L. Miller, "Avalanche breakdown in germanium," *Phys. Rev.*, vol. 99, p. 1234; August 15, 1955.

¹⁷ It is assumed that the collector-to-base junction is essentially a step junction between material of high conductivity on the base side and material of low conductivity on the collector side. The reciprocal dependence of maximum current density and breakdown voltage can be demonstrated for graded and intrinsic barriers as well. Power density limitations implicit in this reciprocity will be the subject of a later paper.

The product $C_{ca}\tau_{ec}$ can be written:

$$C_{ca}\tau_{ec} = \frac{\epsilon}{2v_{sc} \lim} \left[1 + \frac{2v_{sc} \lim}{x_m} \left(\frac{kT}{qJ_E} C_{ca} + \frac{w^2}{nD_{pb}} \right) \right]. \quad (8)$$

Since the second term in the bracket is inherently positive, $C_{ca}\tau_{ec}$ cannot be less than $\epsilon/2v_{sc} \lim$. The physical sense of (8) is that, on a fixed area (one-dimensional) basis, collector capacitance can be reduced only by thickening the collector depletion layer, thus increasing carrier transit time and therefore emitter to collector signal delay time. Detailed calculation finds actual minima about twice this big for a wide range of x_m values. In short, in optimum gain-band designs, C_{ca} and τ_{ec} have a nearly constant product (C_c and f_a in constant ratio).

The remaining one-dimensional parameter, base layer sheet resistance R_{\square} depends on the total number of impurity centers per cm^2 of base layer area ($N_{Db}w$) and on majority carrier mobility μ_{nb} in the base layer

$$R_{\square} = \frac{1}{q\mu_{nb}N_{Db}w}. \quad (9)$$

Increase of N_{Db} usually decreases μ_{nb} (and also D_{pb}) because of increased coulomb scattering of carriers.

MINIMUM $R_{\square}C_{ca}\tau_{ec}$

Minimum values for the parameter $R_{\square}C_{ca}\tau_{ec}$ have been found, assuming:

- 1) given values of N_{Ac} ;
- 2) $J_E = 0.5$ of J_{\max} given by (7);
- 3) collector-to-base junction is a step junction lying largely on the collector side of the p - n transition;
- 4) x_m is that for $V_C = 0.3BV_{CB}$ (BV_{CB} from Miller¹⁴);
- 5) $N_{Db}w = 10^{13}$ donors/ cm^2 of base;
- 6) μ_{nb} and D_{pb} vary as $N_{Db}^{-1/3}$;
- 7) mobilities from the work of Prince and others;¹⁶
- 8) impurity density in the base layer is constant rather than graded;
- 9) the emitter to base barrier is a step with very high concentration on the emitter side and a lower concentration on the base side, uniform in the barrier region.

If, under these assumptions, the $R_{\square}C_{ca}\tau_{ec}$ product obtained by multiplying (8) by (9) is differentiated with respect to base thickness w , a minimum is found when base transit time is:

$$\frac{w^2}{nD_b} \approx \frac{1}{4} \left(\frac{x_m}{2v_{sc} \lim} \right) + \frac{5}{8} \left(\frac{kT}{qJ_E} C_{ca} \right). \quad (10)$$

The numerical constants in (10) are quite sensitive to the assumed mobility variation with N_{Db} . The minima in $R_{\square}C_{ca}\tau_{ec}$ are only slightly sensitive to this assumption.

Table I shows variation of $R_{\square}C_{ca}\tau_{ec}$ with assumed N_{Ac} . The effect on (power gain)^{1/2} (bandwidth) is given by:

¹⁶ M. B. Prince, "Drift mobilities in germanium," *Phys. Rev.*, vol. 92, pp. 681-687; November 1, 1953.

TABLE I

DEPENDENCE OF $R_{\square}C_{ca}\tau_{ec}$ AND GAIN-BAND ON COLLECTOR IMPURITY CONCENTRATION

N_{Ac} Acc/cm ³	$R_{\square}C_{ca}\tau_{ec}$ sec ² /cm ²	$K \equiv (\text{P.G.})^{1/2}(\text{B.W.})$ cps
10^{14}	$.654 \times 10^{-16}$	$12 \times 10^6/s$
10^{15}	1.11×10^{-16}	$9.26 \times 10^6/s$
10^{16}	2.2×10^{-16}	$6.56 \times 10^6/s$
10^{17}	3.88×10^{-16}	$5 \times 10^6/s$

TABLE II

CALCULATED TRANSISTOR DESIGN

Collector Design				Performance		
s	N_{Ac}	x_m	BV_{CB}	f_T	$(\text{P.G.})^{1/2}$ (B.W.)	Impedance Ratio (Com. Em.)
microns	$10^{16}/\text{cm}^3$	10^{-4} cm	volts	kmc	kmc	R_{out}/R_{in}
25	0.1	8.36	140	1.0	3.7	~ 55
25	0.39	2.62	52	3.0	3.0	4.0
25	0.72	1.52	33	5.0	2.72	1.2
7.5	0.39	2.62	52	3.0	10.0	38
7.5	1.72	0.72	17	10.0	7.95	2.2
2.5	1.72	0.72	17	10.0	23.8	22.7
2.5	10.6	0.15	4.5	40.0	20.0	1.0

$$K \equiv (\text{power gain})^{1/2}(\text{bandwidth}) \approx \frac{(5-12) \times 10^6}{s} \text{ cps} \quad (11)$$

where s is stripe width in cm.

PARTICULAR DESIGNS

Table II shows critical parameters of some theoretical transistor designs calculated by interpolation in Table I and related computations. Note that transformers are required to utilize the gain-band product unless the characteristic frequency $f_T \equiv 1/(2\pi\tau_{ec})$ is set at about twice the (power gain)^{1/2}(bandwidth) product.¹⁷

The decrease in (power gain)^{1/2}(bandwidth) with increase of f_T (therefore increase of f_a) is caused by the decrease in base region carrier mobility resulting from coulomb scattering in thin, heavily doped layers. It should be noted that reverse emitter breakdown voltage also decreases as base layer impurity concentration is increased. For the design with f_T of 40 kmc, the residual emitter barrier voltage is little over 0.1 volt and the emitter barrier capacitance is computed to be greater than $1 \mu\text{f}/\text{cm}^2$. These theoretical calculations suggest that transistors usable in the microwave range may be feasible. Fabrication of 2.5 micron wide electrodes will pose some interesting mechanical and electrical problems. It should be noted that the impurity density per square centimeter of base layer which was assumed is moderate rather than very high and that experimental work may possibly yield somewhat better

¹⁷ Note that for this condition $r_b C_c \approx \tau_{ec}$. This makes common emitter input impedance (r_b) equal to output impedance τ_{ec}/C_c . Conversely note that when τ_{ec} is $> r_b C_c$ output impedance is higher than input impedance, but that breakdown voltage is higher and the gain-band product slightly larger.

gain-band figures of merit. The concentration of ac emission in the portions of the emitter nearest the base contacts may also increase the gain-band product.¹⁸

EXPERIMENTAL

Experience has shown that germanium *p-n-p* diffused base transistors with a 25 micron wide emitter stripe and a base contact stripe of equal width 12 to 20 microns away from one edge frequently can be made to oscillate at above 1000 mc. In terms of the model studied, this emitter stripe is 50 microns wide and the stripe-to-stripe spacing is a little below the 1 to 2 ratio assumed in the analysis. Base layer impurity concentrations were probably somewhat higher than those assumed in the analysis. On the other hand, the ratio of collector barrier width to base layer thickness was nowhere near optimum and the collector body is usually about 75 microns thick rather than the less than 10 microns assumed in analysis. Fig. 3 shows emitter and base electrodes of such a transistor and the 10 micron diameter contact wires to the electrodes.

The feasibility of 7.5 microns wide electrodes may, of course, be questioned. Experimental electrodes of this width are shown in Fig. 4. Whether the 2.5 micron wide electrodes are more than a designer's dream remains to be seen.

SUMMARY AND COMPARISON

Analysis shows that the (power gain)^{1/2} (bandwidth) product of a junction triode transistor with linear emitter and base electrodes is inversely proportional to emitter stripe width s (which includes emitter to base spacing). For *p-n-p* germanium devices, the optimum gain-band product is about $7.5 \times 10^6/s$ cps, where s is in centimeters. In addition, this gain-band product, which is approximately the same as the maximum frequency of oscillation, is reciprocal to the square root of the product of base layer sheet resistance, collector capacitance per unit area, and emitter-to-collector delay time. The reciprocity of collector capacitance per unit area and carrier drift time through the collector depletion layer make this product nearly independent of the alpha cutoff frequency of the transistor. An essentially similar value of gain-band product is expected for *n-p-n* germanium transistors, while that for silicon devices is probably a factor of two or more smaller.

The field effect transistor structure analyzed by Dacey and Ross resembles the junction triode structure of Fig. 1 in several ways.² The most important of the similarities is that the electrode which determines the gain-band product in the field effect unit is also a long narrow stripe with ohmic contacts closely spaced on either side. Dacey and Ross derived for the field effect unit a gain-band equation fully comparable to (11):

$$f_{\max} = 5.7 \times 10^5/L \text{ cps} \quad (12)$$

¹⁸ R. L. Pritchard, "High-frequency power gain of junction transistors," *Proc. IRE*, vol. 43, pp. 1075-1085; September, 1955.

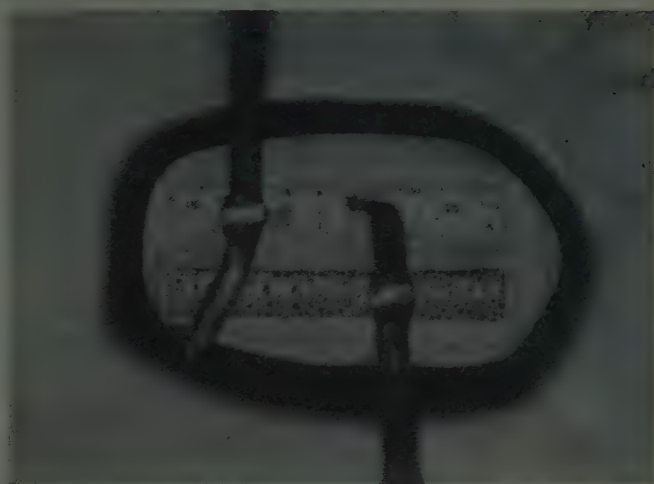


Fig. 3—Top view of experimental diffused base germanium transistor showing 1×6 mil electrodes and 0.4 mil connecting wires.

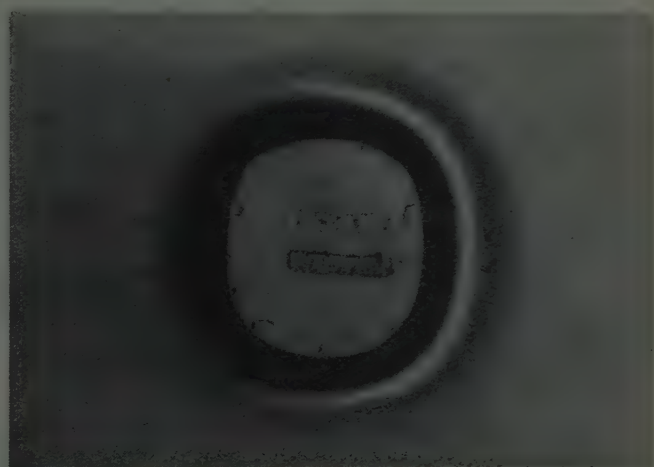


Fig. 4—Top view of experimental diffused base germanium transistor showing 0.3×1.5 mil emitter electrode and base contact.

where L is the width of this gate electrode in centimeters. Although improved impurity distributions might raise this figure of merit for the field effect transistor, it seems doubtful that a factor of 10 could be achieved. The most detailed available theory of the analog transistor⁴ does not contain an expression as fully worked out as that of Dacey and Ross, but there seems no obvious reason for supposing that this device has a better figure of merit than the field effect transistor. Like the junction triode, the field effect has the advantage of operating with most of the active carriers in a space charge neutral region.

Of the three major high frequency three-terminal semiconductor devices, the junction triode appears to have the best inherent gainband product and may well be suitable for some microwave applications.

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58 IRE 3. S1

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I. INTRODUCTION

THIS standard is issued to supersede 54 IRE 3. S1, "IRE Standards on Audio Techniques: Definitions of Terms, 1954," to include the definitions in the 1954 standard and to add definitions of other terms for which it was felt a need exists for establishment of precise and concise meanings. Some of the previous standard definitions have been modified slightly to bring them into uniformity with the added definitions.

The definitions included in this standard all refer specifically to the use of the terms in audio techniques. Many of these terms are used in other fields with different meanings, and it is assumed that definitions for these terms in those fields are or will be included in standards issued by other technical committees. Therefore, in general, the modifying phrase "In Audio Techniques" has been omitted except in certain special cases where it appears to be particularly necessary to avoid confusion.

Terms used within definitions and shown in italics are defined elsewhere in this standard.

II. DEFINITIONS

Active Transducer. See *Transducer, Active*.

Amplification. General transmission term used to denote an increase of *Signal* magnitude.

Amplifier. A device which enables an input *Signal* to control a *Source* of power, and thus is capable of delivering at its output an enlarged reproduction of the essential characteristics of the *Signal*.

Note: Typical amplifying elements are electron tubes, transistors, and magnetic circuits.

Amplifier, Bridging. An *Amplifier* with an *Input Impedance* sufficiently high that its input may be bridged across a circuit without substantially affecting the *Signal Level* of the circuit across which it is bridged.

Amplifier, Clipper. An *Amplifier* designed to limit the instantaneous value of its output to a predetermined maximum.

Amplifier, Distribution. A *Power Amplifier* designed to energize a speech or music distribution system and having sufficiently low *Output Impedance* so that changes in *Load* do not appreciably affect the output voltage.

Amplifier, Isolation. An *Amplifier* employed to minimize the effects of a following circuit on the preceding circuit.

Amplifier, Line. An *Amplifier* which supplies a *Program* transmission line or a system with a *Signal* at a specified *Level*.

Amplifier, Monitoring. A *Power Amplifier* used primarily for evaluation and supervision of a *Program*.

Amplifier, Peak Limiting. See *Peak Limiter*.

Amplifier, Power. An *Amplifier* which drives a utilization device, such as a loudspeaker.

Amplifier, Program. See *Amplifier, Line*.

Amplitude Distortion. See *Distortion, Harmonic and Distortion, Intermodulation*.

Amplitude-Frequency Distortion. See *Distortion, Amplitude-Frequency*.

Amplitude-Frequency Response. The variation of *Gain*, *Loss*, *Amplification*, or *Attenuation* as a function of frequency.

Note: This response is usually measured in the region of operation in which the transfer characteristic of the system or component is essentially linear.

Amplitude Range. The ratio, usually expressed in decibels, between the upper and lower limits of *Program* amplitudes which contain all significant energy contributions.

Attack Time. The interval required, after a sudden increase in input *Signal* amplitude to a system or component, to attain a specified percentage (usually 63 per cent) of the ultimate change in *Amplification* or *Attenuation* due to this increase.

Attenuation. General transmission term used to denote a decrease of *Signal* magnitude.

Attenuator. An adjustable passive device for reducing the amplitude of a *Signal* without introducing appreciable distortion.

Audio Frequency. Any frequency corresponding to a normally audible sound wave.

Audio-Frequency Noise. Any electrical disturbance in the *Audio-Frequency* range introduced from a source extraneous to the *Signal*.

Audio-Frequency Response. See *Amplitude-Frequency Response*.

Audio Oscillator. A nonrotating device for producing *Audio-Frequency* alternating current, the frequency of which is determined by the characteristics of the device.

Audio Spectrum. The continuous range of frequencies extending from the lowest to the highest *Audio Frequency*.

Automatic Gain Control (AGC). A process by which *Gain* is automatically adjusted as a function of input or other specified parameter.

Automatic Volume Control (AVC). A process by which a substantially constant output *Volume* is automatically maintained in a system or component.

Available Power (of a Linear Source of Electric Energy). The power which a *Source* is capable of delivering into its *Conjugate Impedance*.

Note: *Available Power* is equal to the quotient of the mean square of the open-circuit terminal voltage of the *Source* divided by four times the resistive component of the impedance of the *Source*.

Babble. The aggregate *Crosstalk* from a large number of channels.

Balanced Amplifier Circuit. An *Amplifier* circuit in which there are two identical transmission paths usually connected so as to operate with the waves in the two paths in phase opposition.

Balanced Circuit. A circuit, the two sides of which are electrically alike and symmetrical with respect to a common reference point, usually ground.

Band-Elimination Filter. See *Filter, Band-Elimination*.

Band-Pass Filter. See *Filter, Band-Pass*.

Bass Boost. A deliberate adjustment of the *Amplitude-Frequency Response* of a system or component to accentuate the lower *Audio Frequencies*.

Bridging. The shunting of one electrical circuit by another.

Bridging Amplifier. See *Amplifier, Bridging*.

Bridging Gain. The ratio of the power a *Transducer* delivers to a specified *Load Impedance* under specified operating conditions, to the power dissipated in the reference impedance across which the input of the *Transducer* is bridged.

Note 1: If the input and/or *Output Power* consist of more than one component, such as multifrequency *Signal* or *Noise*, then the particular components used and their weighting must be specified.

Note 2: This *Gain* is usually expressed in decibels.

Bridging Loss. The ratio of the power dissipated in the reference impedance across which the input of a *Transducer* is bridged, to the power the *Transducer* delivers to a specified *Load Impedance* under specified operating conditions.

Note 1: If the input and/or *Output Power* consist of more than one component, such as multifrequency *Signal* or *Noise*, then the particular components used and their weighting must be specified.

Note 2: This *Loss* is usually expressed in decibels.

Note 3: In telephone practice this term is synonymous with the *Insertion Loss* resulting from bridging an impedance across a circuit.

Clipper Amplifier. See *Amplifier, Clipper*.

Compressor. The combination, in a transmission system of a *Compressor*, for transmitted *Signals* and an *Expander* for received *Signals*.

Note: The purpose of a *Compressor* is to improve the ratio of *Signal* to the interference entering the transmission path between *Compressor* and *Expander*.

Compressor. A *Transducer* which, for a given input *Amplitude Range*, produces a smaller output range.

Note: One type of *Compressor* reduces the *Amplitude Range* as a linear function of the envelope of speech waves.

Conjugate Impedances. See *Impedances, Conjugate*.

Crossover Network. A selective *Network* which divides its audio input into two or more frequency bands for distribution to loudspeakers.

Crosstalk. Electrical disturbances in a communication channel as a result of coupling with other communication channels.

Cue Circuit. A one-way communication circuit used to convey *Program* control information.

Current Amplification. The ratio of the magnitude of the current in a specified *Load Impedance* connected to a *Transducer*, to the magnitude of the current in the input circuit of the *Transducer*.

Note 1: If the input and/or output current consist of more than one component, such as multifrequency *Signal* or *Noise*, then the particular components used and their weighting must be specified.

Note 2: By custom this *Amplification* is often expressed in decibels by multiplying its common logarithm by 20.

Current Attenuation. The ratio of the magnitude of the

current in the input circuit of a *Transducer*, to the magnitude of the current in a specified *Load Impedance* connected to the *Transducer*.

Note 1: If the input and/or output current consist of more than one component, such as multifrequency *Signal* or *Noise*, then the particular components used and their weighting must be specified.

Note 2: By custom this *Attenuation* is often expressed in decibels by multiplying its common logarithm by 20.

Cutoff Frequency. The frequency which delineates a pass band from an adjacent *Attenuation* band of a system or component.

dbm. A symbol for *Power Level* in decibels with reference to a power of 1 milliwatt (0.001 watt).

Decade. The interval between any two quantities having the ratio of 10:1.

De-Emphasis. A process complementary to *Pre-Emphasis*.

Delay Distortion. See *Distortion, Delay*.

Distortion. An undesired change in waveform.

Distortion, Amplitude. See *Distortion, Harmonic* and *Distortion, Intermodulation*.

Distortion, Amplitude-Frequency. *Distortion* due to an undesired *Amplitude-Frequency Response* characteristic.

Distortion, Delay. That form of *Distortion* which occurs when the rate of change of phase shift with frequency of a circuit or system is not constant over the frequency range required for transmission.

Distortion, Frequency. See *Distortion, Amplitude-Frequency*.

Distortion, Harmonic. *Nonlinear Distortion* characterized by the appearance in the output of harmonics of the fundamental frequency when the input wave is sinusoidal.

Distortion, Intermodulation. *Nonlinear Distortion* characterized by the appearance of frequencies in the output, equal to the sums and differences of integral multiples of the component frequencies present in the input wave.

Note: Harmonic components also present in the output are usually not included as part of the *Intermodulation Distortion*. When harmonics are included, a statement to that effect should be made.

Distortion, Nonlinear. *Distortion* caused by a deviation from a linear relationship between the input and output of a system or component.

Distortion, Per Cent Harmonic. A measure of the *Harmonic Distortion* in a system or component, numerically equal to 100 times the ratio of the square root of the sum of the squares of the root-mean-square voltages (or currents) of each of the individual harmonic frequencies, to the root-mean-square voltage (or current) of the fundamental.

Note: It is practical to measure the ratio of the root-mean-square amplitude of the residual harmonic voltages (or currents), after elimination of the fundamental, to the root-mean-square amplitude of the fundamental and harmonic voltages (or currents) combined. This measurement will indicate *Per Cent Harmonic*

Distortion with an error of less than 5 per cent if the magnitude of the *Distortion* does not exceed 30 per cent.

Distortion, Phase. See *Distortion, Phase-Frequency*.

Distortion, Phase-Frequency. *Distortion* due to a lack of direct proportionality of phase shift to frequency over the frequency range required for transmission.

Note 1: *Delay Distortion* is a special case.

Note 2: This definition includes the case of a linear phase-frequency relation with zero-frequency intercept differing from an integral multiple of π .

Distribution Amplifier. See *Amplifier, Distribution*.

Dividing Network (Loudspeaker Dividing Network). See *Crossover Network*.

Dynamic Range. The ratio of the specified maximum *Signal Level* capability of a system or component to its *Noise Level*, usually expressed in decibels.

Echo. A wave which has been reflected or otherwise returned with sufficient magnitude and delay to be perceived in some manner as a wave distinct from that directly transmitted.

Equalizer. A passive device designed to compensate for an undesired amplitude-frequency and/or phase-frequency characteristic of a system or component.

Expander. A *Transducer* which, for a given input *Amplitude Range*, produces a larger output range.

Note: One type of *Expander* increases the *Amplitude Range* as a linear function of the envelope of speech waves.

Filter. A selective *Network* which transmits alternating currents of desired frequencies and substantially attenuates all others.

Filter, Band-Elimination. A *Filter* which attenuates alternating currents between given upper and lower *Cutoff Frequencies* and transmits substantially all others.

Filter, Band-Pass. A *Filter* which transmits alternating currents between given upper and lower *Cutoff Frequencies* and substantially attenuates all others.

Filter, High-Pass. A *Filter* which transmits alternating currents above a given *Cutoff Frequency* and substantially attenuates all others.

Filter, Low-Pass. A *Filter* which transmits alternating currents below a given *Cutoff Frequency* and substantially attenuates all others.

Filter, Sound Effects. A *Filter*, usually adjustable, designed to reduce the pass band of a system at low and/or high frequencies in order to produce special effects.

Frequency Distortion. See *Distortion, Amplitude-Frequency*.

Frequency Response. See *Amplitude-Frequency Response*.

Gain (Transmission Gain). General term used to denote an increase in *Signal* power in transmission from one point to another. *Gain* is usually expressed in decibels and is widely used to denote *Transducer Gain*.

Gain Control. A device for adjusting the *Gain* of a system or component.

Harmonic Distortion. See *Distortion, Harmonic*.

High-Pass Filter. See *Filter, High-Pass*.

Hiss. Random *Noise* in the *Audio-Frequency* range, having subjective characteristics analogous to prolonged sibilant sounds.

Hybrid Coil. A single transformer which performs the essential function of a *Hybrid Set*.

Hybrid Set. Two or more transformers interconnected to form a *Network* having four pairs of accessible terminals to which may be connected four impedances so that electrical energy introduced into the *Network* at any one pair of terminals ideally divides between two of the other pairs with no transfer of energy to the fourth.

Hum. Electrical disturbance at the power supply frequency or harmonics thereof.

Ideal Transducer. See *Transducer, Ideal*.

Ideal Transformer. See *Transformer, Ideal*.

Image Impedances. See *Impedances, Image*.

Impedance, Input. The impedance presented by the *Transducer* to a *Source*.

Impedance, Iterative. That impedance which, when connected to one pair of terminals of a *Transducer*, produces an identical impedance at the other pair of terminals.

Note 1: It follows that the *Iterative Impedance* of a *Transducer* is the same as the impedance measured at the input terminals when an infinite number of identically similar *Transducers* are formed into an iterative or recurrent structure of infinite length by connecting the output terminals of the first *Transducer* to the input terminals of the second, the output terminals of the second to the input terminals of the third, etc.

Note 2: The *Iterative Impedances* of a four-terminal *Transducer*, are, in general, not equal to each other but for any symmetrical *Transducer* the *Iterative Impedances* are equal and are the same as the *Image Impedances*. The *Iterative Impedance* of a uniform line is the same as its characteristic impedance.

Impedance, Load. The impedance presented by the *Load* to a *Transducer*.

Impedance, Output. The impedance presented by the *Transducer* to a *Load*.

Impedance, Source. The impedance presented by the *Source* to a *Transducer*.

Impedances, Conjugate. Impedances having resistive components which are equal, and reactive components which are equal in magnitude but opposite in sign.

Impedances, Image. The impedances which will simultaneously terminate all inputs and outputs of a *Transducer* in such a way that at each of its inputs and outputs the impedances in both directions are equal.

Note: The *Image Impedances* of a four-terminal *Transducer* are, in general, not equal to each other, but for any symmetrical *Transducer*, the *Image Impedances* are equal, and are the same as the *Iterative Impedances*.

Input Impedance. See *Impedance, Input*.

Insertion Gain. Resulting from the insertion of a *Transducer* in a transmission system, the ratio of the power

delivered to that part of the system following the *Transducer* to the power delivered to that same part before insertion of the *Transducer*.

Note 1: If the input and/or *Output Power* consist of more than one component, such as multifrequency *Signal* or *Noise*, then the particular components used and their weighting must be specified.

Note 2: This *Gain* is usually expressed in decibels.

Note 3: The "insertion of a *Transducer*" includes bridging of an impedance across the transmission system.

Insertion Loss. Resulting from the insertion of a *Transducer* in a transmission system, the ratio of the power delivered to that part of the system following the *Transducer*, before insertion of the *Transducer*, to the power delivered to that same part of the system after insertion of the *Transducer*.

Note 1: If the input and/or *Output Power* consist of more than one component, such as multifrequency *Signal* or *Noise*, then the particular components used and their weighting must be specified.

Note 2: This *Loss* is usually expressed in decibels.

Note 3: The "insertion of a *Transducer*" includes bridging of an impedance across the transmission system.

Intermodulation Distortion. See *Distortion, Intermodulation*.

Isolation Amplifier. See *Amplifier, Isolation*.

Isolation Transformer. See *Transformer, Isolation*.

Iterative Impedance. See *Impedance, Iterative*.

Level. The difference of a quantity from an arbitrarily specified reference quantity.

Note: The quantities of interest are often expressed in decibels, thus their difference is conveniently expressed as a ratio. Hence, *Level* is widely regarded as the ratio of the magnitude of a quantity to an arbitrary reference magnitude.

Line Amplifier. See *Amplifier, Line*.

Line Transformer. See *Transformer, Line*.

Load. 1) The device which receives *Signal* power from a *Transducer*.

2) The *Signal* power delivered by a *Transducer* (deprecated).

Load Impedance. See *Impedance, Load*.

Loss (Transmission Loss). General term used to denote a decrease in *Signal* power in transmission from one point to another. *Loss* is usually expressed in decibels.

Low-Pass Filter. See *Filter, Low-Pass*.

Microphonics. *Audio-Frequency Noise* caused by mechanical vibration of elements in a system or component.

Mixer (in Audio Techniques). A device, having two or more inputs and a common output, which operates to combine linearly in a desired proportion the separate input *Signals* to produce an output *Signal*.

Monitoring Amplifier. See *Amplifier, Monitoring*.

Motorboating. Oscillation in a system or component,

usually manifested by a succession of pulses occurring at a sub-audio or low-audio repetition frequency.

Network. A combination of electrical elements.

Noise. See *Audio-Frequency Noise*.

Nonlinear Distortion. See *Distortion, Nonlinear*.

Octave. The interval between any two frequencies having a ratio of 2:1.

Output Impedance. See *Impedance, Output*.

Output Power. The power delivered by a system or component to its *Load*.

Pad. A nonadjustable passive device for reducing the amplitude of a *Signal* without introducing appreciable *Distortion*.

Passive Transducer. See *Transducer, Passive*.

Peak Limiter. A device which automatically limits the magnitude of a *Signal* to a predetermined maximum value in accordance with a specified *Attack Time* and a specified *Recovery Time*.

Peak Limiting Amplifier. See *Peak Limiter*.

Per Cent Harmonic Distortion. See *Distortion, Per Cent Harmonic*.

Phase Distortion. See *Distortion, Phase-Frequency*.

Phase-Frequency Distortion. See *Distortion, Phase-Frequency*.

Power Amplifier. See *Amplifier, Power*.

Power Gain. The ratio of the power that a *Transducer* delivers to a specified *Load*, under specified operating conditions, to the power absorbed by its input circuit.

Note 1: If the input and/or *Output Power* consist of more than one component, such as multifrequency *Signal* or *Noise*, then the particular components used and their weighting must be specified.

Note 2: This *Gain* is usually expressed in decibels.

Power Level. At any point in a transmission system, the difference of the measure of the steady-state power at that point from the measure of an arbitrarily specified amount of power chosen as a reference.

Note: The measures are often expressed in decibels, thus their difference is conveniently expressed as a ratio. Hence, *Power Level* is widely regarded as the ratio of the steady-state power at some point in a system to an arbitrary amount of power chosen as a reference.

Power Loss. The ratio of the power absorbed by the input circuit of a *Transducer* to the power delivered to a specified *Load* under specified operating conditions.

Note 1: If the input and/or *Output Power* consist of more than one component, such as multifrequency *Signal* or *Noise*, then the particular components used and their weighting must be specified.

Note 2: This *Loss* is usually expressed in decibels.

Preamplifier. An *Amplifier*, the primary function of which is to raise the output of a low-level source to an intermediate *Level* so that the *Signal* may be further processed without appreciable degradation in the signal-to-noise ratio of the system.

Note: A *Preamplifier* may include provision for equalizing and/or mixing.

Pre-Emphasis. A process in a system designed to emphasize the magnitude of some frequency components with respect to the magnitude of others.

Note: *Pre-Emphasis* at the transmitting end of a system, in conjunction with *De-Emphasis* at the receiving end, is applied for the purpose of improving signal-to-noise ratio.

Program. A sequence of audio signals transmitted for entertainment or information.

Program Amplifier. See *Amplifier, Line*.

Program Level. The measure of the *Program Signal* in an audio system expressed in *vu*.

Push-Pull Amplifier Circuit. See *Balanced Amplifier Circuit*.

Recovery Time. The interval required, after a sudden decrease in *Input Signal* amplitude to a system or component, to attain a specified percentage (usually 63 per cent) of the ultimate change in *Amplification* or *Attenuation* due to this decrease.

Reference Volume. The *Volume* which gives a reading of 0 *vu* on a *Standard Volume Indicator*.

Remote Line. A *Program* transmission line between a remote-pickup point and the studio or transmitter site.

Roll-Off. A gradually increasing *Loss* or *Attenuation* with increase or decrease of frequency beyond the flat portion of the *Amplitude-Frequency Response* characteristic of a system or component.

Signal. 1) A visual, audible, or other indication used to convey information.
2) The intelligence, message, or effect to be conveyed over a communication system.
3) A *Signal* wave.

Signal Level. At any point in a transmission system, the difference of the measure of the *Signal* at that point from the measure of an arbitrarily specified *Signal* chosen as a reference.

Note: The measures of the *Signal* are often expressed in decibels, thus their difference is conveniently expressed as a ratio.

Singing. An undesired self-sustained oscillation in a system or component.

Note: This term implies oscillation at a frequency in or above the pass band of the system or component.

Singing Margin. The difference in *Level*, usually expressed in decibels, between the *Singing Point* and the operating *Gain* of a system or component.

Singing Point. The minimum value of *Gain* of a system or component that will result in *Singing*.

Single-Ended Push-Pull Amplifier Circuit. An *Amplifier* circuit having two transmission paths designed to operate in a complementary manner and connected so as to provide a single unbalanced output.

Note: This circuit provides push-pull operation without the use of a transformer.

Sound Effects Filter. See *Filter, Sound Effects*.

Source. The device which supplies *Signal* power to a *Transducer*.

Source Impedance. See *Impedance, Source*.

Standard Volume Indicator. A device for the indication of *Volume* having the characteristics prescribed in ASA-C16.5.

Thump. A low-frequency transient disturbance in a system or component characterized audibly by the onomatopoeic connotation of the word.

Transducer. A device capable of being actuated by waves from one or more transmission systems or media and of supplying related waves to one or more other transmission systems or media.

Transducer, Active. A *Transducer* whose output waves are dependent upon sources of power, apart from that supplied by any of the actuating waves, which power is controlled by one or more of these waves.

Transducer, Ideal (for Connecting a Specified Source to a Specified Load). A hypothetical passive *Transducer* which transfers the maximum possible power from the source to the *Load*.

Note: In linear *Transducers* having only one input and one output, and for which the impedance concept applies, this is equivalent to a *Transducer* which a) dissipates no energy and b) when connected to the specified *Source* and *Load* presents to each its *Conjugate Impedance*.

Transducer, Passive. A *Transducer* whose output waves are independent of any sources of power which are controlled by the actuating waves.

Transducer Gain. The ratio of the power that the *Transducer* delivers to a specified *Load* under specified operating conditions to the *Available Power* of a specified *Source*.

Note 1: If the input and/or *Output Power* consist of more than one component, such as multifrequency *Signal* or *Noise*, then the particular components used and their weighting must be specified.

Note 2: This *Gain* is usually expressed in decibels.

Transducer Loss. The ratio of the available power of a specified *Source* to the power that the *Transducer* delivers to a specified *Load* under specified operating conditions.

Note 1: If the input and/or *Output Power* consist of more than one component, such as multifrequency *Signal* or *Noise*, then the particular components used and their weighting must be specified.

Note 2: This *Loss* is usually expressed in decibels.

Transformer, Ideal. A hypothetical transformer which neither stores nor dissipates energy. Its self-inductances have a finite ratio and unity coefficient of coupling. Its self and mutual impedances are pure inductances of infinitely great value.

Transformer, Isolation. A transformer inserted in a system to separate one section of the system from undesired influences of other sections.

Transformer, Line. A transformer inserted in a system for such purposes as isolation, impedance matching or additional circuit derivation.

Transformer Loss. The ratio of the power that would be delivered to a specified *Load Impedance* if an *Ideal*

Transformer were substituted for the actual transformer, to the power delivered to the specified *Load Impedance* by the actual transformer, under the condition that the impedance ratio of the *Ideal Transformer* is equal to that specified for the actual transformer.

Note 1: If the input and/or *Output Power* consist of more than one component, such as multifrequency *Signal* or *Noise*, then the particular components used and their weighting must be specified.

Note 2: This *Loss* is usually expressed in decibels. **Transformer Loss (Deprecated).** The *Loss* which would be eliminated by the insertion, at any point in a transmission system, of an *Ideal Transformer* having an impedance ratio equal to the absolute value of the ratio of the impedances facing the actual transformer.

Note: This *Loss* is usually expressed in decibels.

Transition Loss. At any point in a transmission system, the ratio of the *Available Power* from that part of the system ahead of the point under consideration to the power delivered to that part of the system beyond the point under consideration.

Note 1: If the input and/or *Output Power* consist of more than one component, such as multifrequency *Signal* or *Noise*, then the particular components used and their weighting must be specified.

Note 2: This *Loss* is usually expressed in decibels. **Treble Boost.** A deliberate adjustment of the *Amplitude-Frequency Response* of a system or component to accentuate the higher *Audio Frequencies*.

Unbalanced Circuit. A circuit, the two sides of which are electrically unlike.

Voltage Amplification. The ratio of the magnitude of the voltage across a specified *Load Impedance* connected to a *Transducer* to the magnitude of the voltage across the input of the *Transducer*.

Note 1: If the input and/or output voltage consist of more than one component, such as multifrequency

Signal or *Noise*, then the particular components used and their weighting must be specified.

Note 2: By custom this *Amplification* is often expressed in decibels by multiplying its common logarithm by 20.

Voltage Attenuation. The ratio of the magnitude of the voltage across the input of the *Transducer* to the magnitude of the voltage delivered to a specified *Load Impedance* connected to the *Transducer*.

Note 1: If the input and/or output voltage consist of more than one component, such as multifrequency *Signal* or *Noise*, then the particular components used and their weighting must be specified.

Note 2: By custom this *Attenuation* is often expressed in decibels by multiplying its common logarithm by 20.

Volume. The magnitude of a complex *Audio-Frequency* wave in an electric circuit as measured on a *Standard Volume Indicator*. The *Volume* is expressed in *vu*. In addition, the term *Volume* is used loosely to signify either the intensity of a sound or the magnitude of an *Audio-Frequency* wave.

Volume Control. See *Gain Control*.

Volume Indicator. See *Standard Volume Indicator*.

Volume Limiter (Deprecated). See *Peak Limiter*.

vu. A quantitative expression for *Volume* in an electric circuit.

Note 1: *vu* is pronounced "vee-you" and customarily written with lower case letters.

Note 2: The *Volume* in *vu* is numerically equal to the number of decibels which expresses the ratio of the magnitude of the waves to the magnitude of *Reference Volume*.

Note 3: The term *vu* should not be used to express results of measurements of complex waves made with devices having characteristics differing from those of the *Standard Volume Indicator*.

Frequency Variations in Short-Wave Propagation*

TORU OGAWA†, MEMBER, IRE

Summary—Frequency variations in the propagation of short-wave signals were observed at frequencies of 5 mc and 10 mc for about six months, beginning in August, 1957, utilizing the standard frequency transmission of station JJY in Tokyo. The distance from the station to the receiving point was about 360 km, and the propagation path was nearly parallel to the latitude. It was found that during the six to ten-hour period centered at noon the *E*-layer reflection of 5 mc was most suitable for utilizing the standard frequency, although

the field intensity was very weak and the accuracy of the frequency comparison was only 5×10^{-3} , which was inferior by about a factor of ten to that possible with the VLF standard signals.

The propagation of signals (at 5 mc at night and 10 mc throughout 24 hours) which are widely used for communication service was accompanied by considerably large frequency variations, up to 3×10^{-7} . However, most variations are not large enough to disturb the communication quality even for those communication systems which require the severest limitation of frequency variations.

The diurnal and seasonal variations of the 5-mc signals, whose reflection point was in the *E* layer in the daytime and in the *F*₂ layer

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at night, were observed, and the differences between the F_2 - to E -layer exchange in the morning and the E - to F_2 -layer exchange at evening were also observed and discussed.

It was found by simultaneous observations of 5-mc and 10-mc signals that the long period movements at local points in the F_2 layer seemed to be nearly always correlated with each other.

The apparatus used is described and its limitations are discussed.

INTRODUCTION

THE information obtained from the observation of frequency variations in short-wave propagation is divided principally into three classes. The first class considers the utility of the standard frequency transmissions, since the observed variations of up to 3×10^{-7} caused in the propagation path were so large compared with the variations of the standard frequency itself. (These latter variations are small multiples of 10^{-9} at the transmitter.)¹ The second class of information is related to the distortion in special communication systems. In the rather serious case of the SSB system, the variations could be large enough to disturb the transmission quality, since the allowable value of the variation without considerable distortion has been measured as 2 cycles, *i.e.*, 2×10^{-7} at 10 mc.² In the future this effect will become more serious in the problem of communication quality, because it will be necessary to reduce the bandwidth more and more in order to avoid congestion in communications. As to the transmission of standard frequency signals, those in the VLF band were surprisingly superior to the ones in the HF band,³ in which most standard frequency stations are now operated; therefore the VLF band may be used increasingly. However, it is impractical for commercial communications to change to the VLF band, since its usable frequency bandwidth is very narrow. The third class of information concerns the instability of the ionosphere. The vertical velocity of position of the same electron density can be directly and continuously observed by measuring the frequency variations in the propagation, and the velocity can be measured to an accuracy of 1 m/s or smaller. Therefore, the fine and sudden disturbances in the ionosphere can also be observed.

Frequency variations in short-wave propagation have been observed by several authors for rather short periods,⁴⁻⁶ and many of these observers placed the empha-

sis on the standard frequency transmission. The present author has constructed an apparatus suitable for the continuous observation and study of the character of frequency variations in relation to the three areas mentioned above.

The frequency variations in propagation are caused by two factors, the Doppler effect at the reflection point and the variations of the group velocity in the ionosphere. The Doppler effect is proportional to the vertical component of the velocity of the point which has enough electron density to reflect the radio wave being considered, and the variations of the group velocity are caused by the variations of electron density from the wave entrance point to the exit point of the ionosphere. These two effects may be summarized in equations. The frequency variation in the total propagation path is expressed as

$$\delta f = f \frac{d}{dl} \int_0^l \frac{dl}{u}, \quad (1)$$

where l is the distance from the transmitting point to the receiving point measured along the propagation path, and u is the group velocity of the radio wave. Neglecting the earth's magnetic field and collision friction, u is given for short waves by

$$u = c \left(1 - \frac{e^2 N}{m \pi f^2} \right)^{1/2}, \quad (2)$$

where c is the velocity of light in free space, e and m are the charge and mass of an electron, respectively, and N is the electron density of the ionosphere. Therefore, assuming the propagation path to be symmetric about the vertical line through the reflection point,

$$\delta f = 2 \frac{f}{c} \frac{d}{dl} \int_0^h \left(1 + \frac{e^2 N}{2 \pi m f^2} \right) \cos i dh, \quad (3)$$

where h is the real height of the reflection point and i is the angle between dl and a line normal to the boundary of the ionosphere. Since (1) can be transformed into an equation involving the familiar variable h' , the virtual height of the reflection point, that is,

$$\delta f = \frac{2f \cos i_0}{c} \frac{dh'}{dl}, \quad (4)$$

where i_0 is the incident angle to the ionosphere, then the frequency variation can also be expressed in terms of the time derivative of the virtual height.

APPARATUS

A block diagram of the apparatus is shown in Fig. 1. The incoming standard frequency from the antenna is mixed at the receiver input with a harmonic frequency of the auxiliary crystal oscillator and then amplified. The auxiliary crystal oscillator is adjusted to a frequency slightly different from a subharmonic of the standard frequency. The output signal of the receiver is again amplified by a selective amplifier, which is fol-

¹ See, *e.g.*, National Bureau of Standards, Boulder Labs., Colo., "Standard frequencies and time signals WWV and WWVH," *PROC. IRE*, vol. 44, pp. 1470-1473; October, 1956.

² See, *e.g.*, N. Koomans, "Single-sideband telephony applied to the radio link between the Netherlands and the Netherlands East Indies," *PROC. IRE*, vol. 26, pp. 182-206; February, 1938.

³ J. A. Pierce, "Intercontinental frequency comparison by very-low-frequency radio transmission," *PROC. IRE*, vol. 45, pp. 794-803; June, 1957.

⁴ L. Essen, "Standard frequency transmission," *Proc. IEE*, vol. 101, pt. 3, pp. 249-255; July, 1954.

⁵ J. M. Steele, "The standard frequency monitor at the National Physical Laboratory," *Proc. IEE*, vol. 102, pt. 2, pp. 155-165; March, 1955.

⁶ I. Takahashi, T. Ogawa, M. Yamano, A. Hirai, and M. Takiuchi, "Doppler shift of the received frequency from the standard station reflected by the ionosphere," *PROC. IRE*, vol. 45, p. 1408; October, 1957.

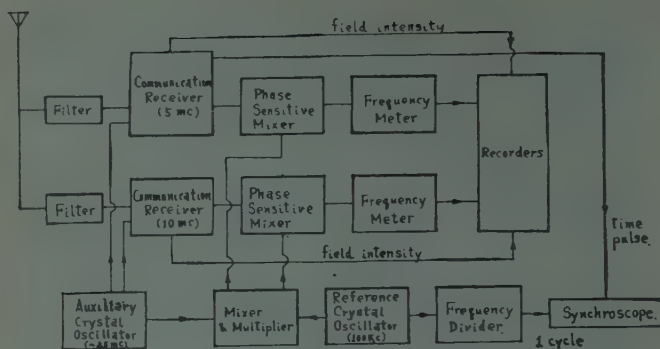


Fig. 1—Block diagram of apparatus.

lowed by the phase sensitive mixer. The output of the auxiliary crystal oscillator is also introduced into the mixer and multiplier in which its harmonics are mixed with a harmonic of a 100-kc reference crystal oscillator. The two beat frequencies are fed into a phase sensitive mixer, producing a frequency which is the difference between the incoming frequency and the harmonics of the reference crystal oscillator. The effect of the variations in the frequency of the auxiliary crystal oscillator is canceled out by this last mixer. The output of the last phase sensitive mixer is introduced into a frequency meter having a high-frequency sensitivity, which can be operated at a frequency of 0.02 cps or lower at a sufficiently large amplitude, and whose output current is proportional to the frequency of the input signal.

The frequency meter is similar in principle to the counting-rate meter,⁷ and its block diagram and waveforms for each stage are shown in Fig. 2. The beat signal is transformed into a rectangular signal by a voltage discriminator, and after differentiation, it drives the univibrator, which produces a constant width pulse per each cycle of the beat frequency. By integrating these pulses, the output direct current becomes proportional to the beat frequency. The frequency sensitivity may be increased by adjusting the width of these pulses.

In the present apparatus, a second channel was added, as shown below the broken line in Fig. 2. The phase of the reference signal fed to the second phase sensitive mixer is shifted about 90° from that of the first mixer. The gate of one channel is opened when that channel is operating, but closed when the other channel is being used. Therefore, when the incoming signal frequency is higher than the harmonics of the reference frequency, only the upper channel is in action while the lower channel is stopped, and vice versa. Therefore, the deflection in the recorder is to the right or to the left according to whether the incoming standard frequency is higher or lower than the harmonics of the reference frequency, respectively; in other words the frequency meter becomes sign sensitive. As a result, it is not necessary for the reference oscillator to be offset from its nominal fre-

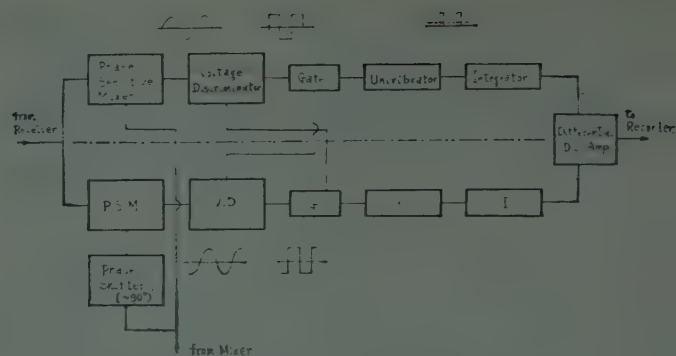


Fig. 2—Block diagram of phase sensitive mixer and frequency meter.

quency so that the pulses generated at the last stage of the frequency divider can be compared with the time signals modulating the standard frequency; also, it is available for other uses. In the comparison of the time signals, the variations caused by the propagation path are integrated over a long time interval—e.g., for 24 hours—and the measuring error becomes very small. However, there are several disadvantages to this method. First, the action threshold voltage of the two discriminators must be adjusted to the same amount when the signal is weak, and second, the closer the beat frequency is to zero, the smaller becomes the voltage-sensitivity of the discriminators. Therefore, in the case of weak signals, it is better that the reference oscillator be offset; in practice the lower channel of the frequency meter was only used in simultaneous operation with the time signal comparison.

The over-all accuracy of the complete apparatus is limited by several factors. The most important one is the accuracy of the reference crystal oscillator, and other ones are the variations of the pulse height and width at the univibrator and the balancing of the direct current amplifier in the frequency meter. The drift of the reference crystal oscillator is measured to be about 1×10^{-8} per day by means of the time comparison between the output pulse of the frequency divider and the standard time signal employing a synchroscope, and by the frequency comparison method utilizing the 5-mc signal received via E-layer reflection. As the errors arising from other factors are much smaller than that of the reference oscillator, the total accuracy is estimated to be about 1×10^{-8} per day, i.e., the error in measurement of the vertical velocity of the reflection point is estimated to be about 1.5 m/s per day in the case of vertical incidence. Of course the total error for a short period is less than this value and is smaller than one meter per second per day.

Such a method, utilizing the frequency meter, is superior to the ordinary beat method^{8,9} in the direct read-

⁷ W. C. Elmore and M. Sands, "Electronics, Experimental Techniques," McGraw-Hill Book Co., Inc., New York, N. Y., pp. 249-256, 1949.

⁸ A. H. Allan, D. D. Crombie, and W. A. Penton, "Frequency variations in New Zealand of 16 kc/s transmission from GBR Rugby," *Nature*, vol. 177, pp. 178-179; January 28, 1956.

⁹ I. Takahashi, T. Ogawa, M. Yamano, A. Hirai, and M. Takayama, "Stark modulation atomic clock," *Rev. Sci. Instr.*, vol. 27, pp. 739-745; September, 1956.

ing of frequency variations. However, the disadvantage is that when the beat frequency becomes very low, the errors of the frequency meter are relatively not negligible. Generally, in frequency comparison it is preferable to employ the frequency meter method when the frequency difference is 0.1 cps or higher, and the ordinary beat method when it is 0.1 cps or lower.

Finally, the field intensity of the received signal can be recorded for assistance in analysis by a calibrated bridge circuit in the receiver.

OBSERVED RESULTS AND DISCUSSION

Observations were made beginning August, 1957, and the frequencies observed were at 5 mc and 10 mc. The observation point was at Doshisha University in Kyoto, Japan, at long. 135.8° E and lat. 35.0° N, which is about 360 km distance from the standard frequency station JJY of the Radio Research Laboratories in Tokyo, Japan, at long. 139.5° E and lat. 35.7° N. As the propagation path was nearly parallel to the latitude, the effects of the extraordinary wave could be neglected.

The frequency variations were almost continuously observed except for the periods of improvement of apparatus, and the field intensity was sometimes observed.

These two frequencies were selected for the following reasons. To use a radio wave signal as the frequency standard, it is important in many cases that the frequency variations caused by the propagation medium be as small as possible even when the field intensity is at its lowest detectable level. Earlier observations have shown that the variations are much smaller in the case of the *E*-layer reflection than in that of the other layers. In the present case, the incident angle to the *E* layer is about 60°; therefore, the radio waves with frequencies higher than about 7 mc cannot be received by *E*-layer reflection during the whole year, except during periods of extraordinary disturbances in the ionosphere. Even if a frequency less than this value is selected, the period of *E*-layer reflection is limited. However, as the frequency is lowered, this time interval increases. From this point of view, the 2.5-mc standard frequency is more suitable than the 5-mc one. However, the field intensity of the former is much smaller than that of the latter due to the increased attenuation of the ionosphere. Also, the standard station JJY is not always on the air at 2.5 mc. The 5-mc signal was selected not only to measure its utility as a standard frequency in the daytime but also as a communication frequency at night, when the frequency variation usually is very large due to the *F*₂-layer disturbances.

The frequency range of 10-mc signals is suitable for long-distance communication in the daytime and also at night. Most domestic radio communication systems whose range is larger than several hundred kilometers are operated in the neighborhood of this frequency, especially in the daytime. Thus, by measuring the frequency variation at 10 mc, the signal distortion of domestic service in the daytime and of intercontinental

service at night may be explained. The 15-mc standard signal might also have been observed as well as the 10 mc, but the analysis of the data was very complex because at this frequency, even in the daytime, the signal intensity of the radio wave from Hawaii (WWVH) becomes stronger than the one from Tokyo (JJY) more frequently than at 10 mc.

Typical examples of the diurnal variations of frequency variation are shown in Fig. 3(a) and (b). The frequency variation record at 5 mc in Fig. 3(a) can be roughly separated into four time intervals. Period I is the six to ten hours centered at about noon, when the received signal is assumed to be the result of *E*-layer reflection, because in this time interval the electron density of the *E* layer is great enough to reflect a 5-mc signal which approaches at an incident angle of about 60°. The good quality of the 5-mc signal in this period is of great interest: it is most suitable as a frequency and time standard transmission, because the frequency variations are very small compared with the other periods of the 5-mc record and the whole part of the 10 mc, as shown in Fig. 3(b). On the days in which the ionosphere disturbances were small, it was possible to compare the standard frequency to the local stable oscillator with a precision up to 5×10^{-9} by a two to three hours frequency comparison. These days were about 75 per cent of the total period of observation. Fig. 4 shows the seasonal variation of such usable time intervals for standard frequency comparison. The two solid lines show the theoretical curves indicating the limiting times for *E*-layer reflection based upon the law that the critical frequency of the *E* layer is proportional to $(\cos \chi)^{1/4}$, where χ is the solar zenith angle. The limiting points observed are almost all located inside but near the theoretical curves. Some of the larger intervals between the theoretical curves and the observed points indicate that the movements of the *E* layer near the beginning and the end of the reflection period became irregular. In Period I the field intensity was so weak, as shown in Fig. 5(a), that it will be difficult to use the radio signals for communication service, even if the frequency variations were small. In Period II most of the frequency variations were of the order of 5×10^{-8} , but were sometimes accompanied by sudden variations of 2×10^7 . Because the electron density of the *E* layer at night decreases to about one tenth of the value in the daytime,¹⁰ the propagation of the 5-mc wave at that time was obviously via the *F*₂ layer. The frequency variations are assumed to depend both upon the variations in the height of the reflection point in the *F*₂ layer and upon the variations of group velocity in the ionosphere. However, the variations of the group velocity cannot possibly cause such large frequency variations for such long time intervals. For example, let us imagine an extreme case in which the height of the reflection point is not changing and the electron density in

¹⁰ A. P. Mitra, "Night-time ionization in the lower ionosphere," *J. Atmos. Terr. Phys.*, vol. 10, pp. 140-162; March, 1957.

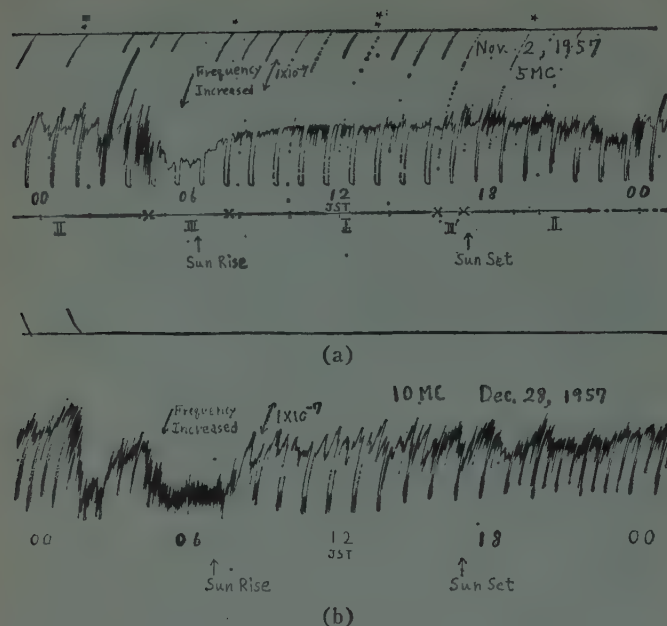


Fig. 3—Typical example of diurnal variation. (a) 5 mc. (b) 10 mc.

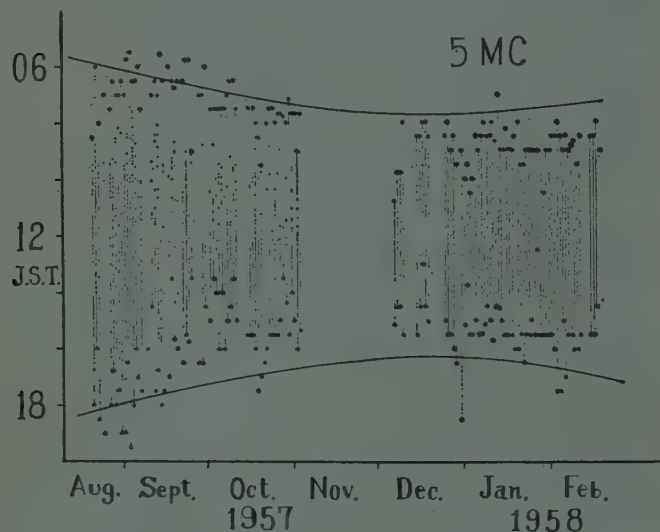


Fig. 4—Seasonal variation of usable time intervals for standard frequency comparison at 5 mc.

the ionosphere below the reflection point, a distance of 10 km, varies uniformly with time from zero to 5×10^4 per cubic centimeter in 5 seconds. For that extreme case, the frequency variation is estimated from (3) to be only about 4×10^{-9} at 5 mc. Consequently, the frequency variations will mainly depend upon the effect of the variations of the reflection point itself. Remarkable variations up to the order of -3×10^{-7} appeared for about one hour between 1 A.M. and 4 A.M. on most days. Although these variations accompany reception of the radio wave from WWVH, the mechanism of their origin is not clear.

In Period III, centered around sunrise, the variations appeared to increase the frequency; the cause of this increase is believed to be the movement of the reflection point from the F_2 layer to the E layer. The frequency

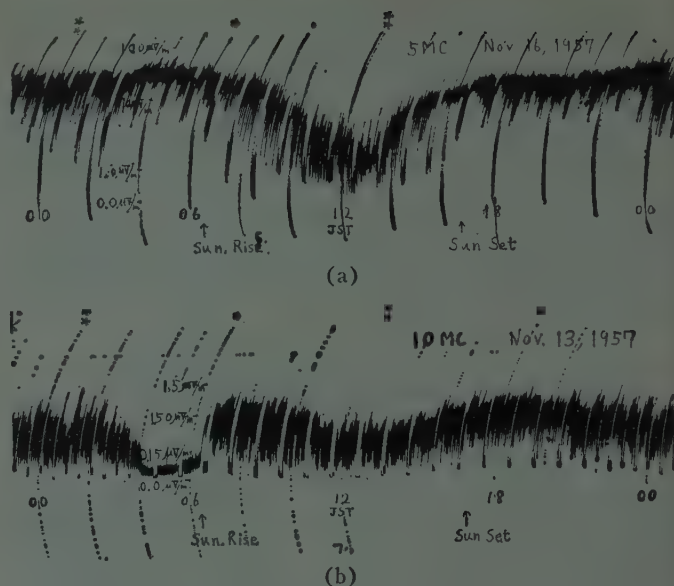


Fig. 5—Typical example of field intensity variations. (a) 5 mc. (b) 10 mc.

change was gradual and reached a value up to about $+1 \times 10^{-7}$. In Period III', which was at sunset, the variations tended to decrease the frequency, although not so much as in Period III; but they were accompanied by sudden variations of short duration. Such variations are believed to be caused by the inverse of the process in Period III, that is, by the reflection point moving from the E layer to the F_2 layer. In the F_2 -to- E -layer change, the reflection point appeared to be coming down at a mean velocity of about 20 m/s, whereas in the E -to- F_2 -layer change the reflection occurs simultaneously at both layers, which are moving up at a velocity somewhat smaller than that mentioned above. In the latter case, the relative field intensities of the waves from the different layers are rapidly alternating in their relative intensities. It is interesting to note that the processes were different for the F_2 -to- E -layer and the E -to- F_2 -layer exchanges.

Except during Period I, the field intensity was sufficient for use in communication service, and was between $10 \mu\text{V/m}$ and 10 mV/m . Fig. 6(a) shows an example of the distribution of the frequency variations at 5 mc, measured at hourly intervals from midnight throughout the day. Although the maximum frequency variations amount to 3×10^{-7} , even those communication systems that allow a variation of only 2 cps may be successfully operated.

The standard frequency station JJY is off the air from 29 minutes to 39 minutes past each hour, and the hourly interruption of the recordings during the daytime due to this are plainly visible. These interruptions on the records were shortened at night by the WWVH transmission, which is off the air for the period between 30 minutes to 34 minutes past each hour, and in some cases by the WWV transmission, which is continuous

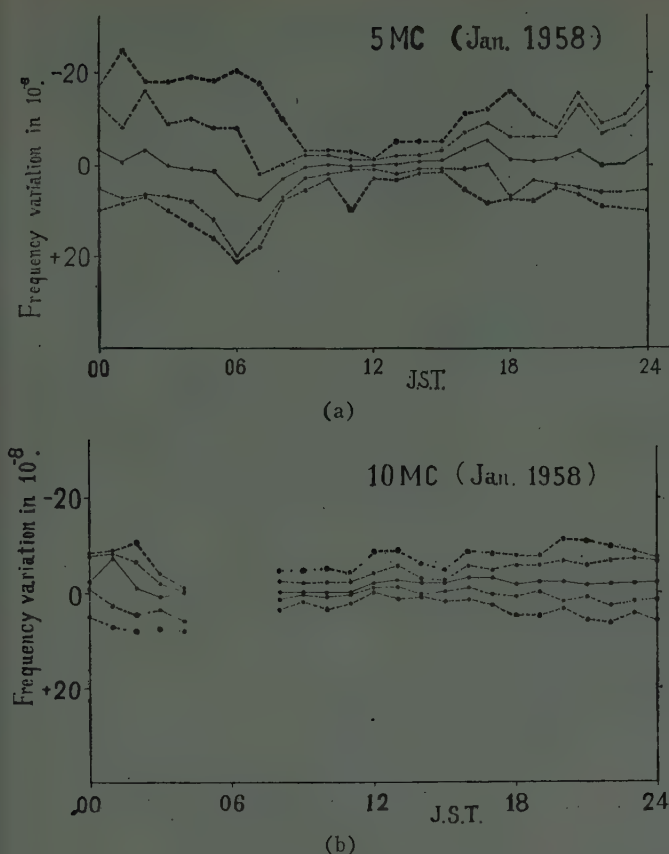


Fig. 6—Distribution of frequency variations. (a) 5 mc. (b) 10 mc. Dotted line, maximum variation; broken line, 90 per cent variation; and solid line, mean variation. (Distributions of 10 mc from 5:00 to 7:00 A.M. could not be obtained according to the penetration of signal.)

during the JJY interruption. It is interesting to observe that the frequency variations of the radio signals from WWVH were of the same order as those from JJY, although the distance of WWVH is about twenty times that of JJY; however the observation period was very much shorter than that for JJY.

Typical examples of frequency variations at 10 mc are shown in Fig. 3(b). At this frequency the changes on the record are not so distinct as at 5 mc, because the reflection of the 10-mc radio wave from JJY and WWVH is always via the F_2 layer, except in the cases of the appearance of a layer having a much larger electron density at or below the height of the F_2 layer. The field intensity dropped to almost zero because of the deep penetration of the signals into the F_2 layer from about 4 A.M. to 6 A.M., as shown in Fig. 5(b); this time interval was, of course, slightly different from day to day. The distribution of frequency variations at 10 mc for each hour is shown in Fig. 6(b); the variations are normally less than 2 cps, although sudden variations amounting to 3 cps do occur at times.

Fig. 7 shows a typical example of simultaneous observation of frequency variations at 5 mc and 10 mc at night. The two almost correlate with each other not only

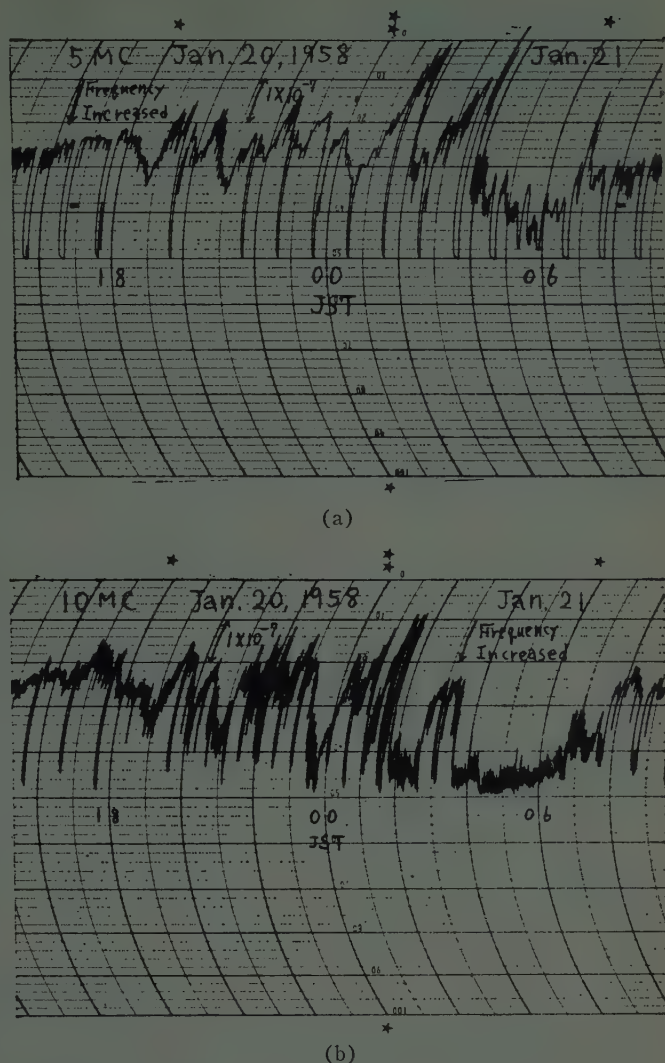


Fig. 7—An example of simultaneous observation of 5-mc and 10-mc signals reflected from the F_2 layer.

in the amount of variation but also in the length of duration, except for those of short duration. Hence it may be concluded that in the F_2 layer at night independent variations of the electron density within small volumes are not very pronounced, but that the variations of the layer as a whole are the dominant phenomena.

It was not completely evident whether any of the frequency variations corresponded closely to the appearance of the sporadic E layer or not. However, several observations around the time of appearance of the sporadic E layer at night showed the frequency variations were of the order 4×10^{-8} and that vertical velocity of the reflection point seemed unexpectedly small at 5 mc. Also, the signal from Hawaii was not received; therefore the signal recordings were similar to those in the daytime.

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IRE Standards on Recording and Reproducing: Methods of Calibration of Mechanically-Recorded Lateral Frequency Records, 1958*

58 IRE 19. S1

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* Approved by the IRE Standards Committee, February 13, 1958. Reprints of this standard, 58 IRE 19. S1, may be purchased while available from the Institute of Radio Engineers, 1 East 79th Street, New York, N. Y., at \$0.60 per copy. A 20 per cent discount will be allowed for 100 or more copies mailed to one address.

I. INTRODUCTION

MECHANICALLY-RECORDED frequency records are made for the purpose of calibrating recording systems and recording heads. Such records are available commercially for testing phonograph pickups and reproducing systems. Usually, a frequency record contains a number of sinusoidal signals of various significant frequencies recorded in separate short bands on the record.

Three basic methods are described in this standard for calibrating laterally-modulated frequency records. The same general techniques also are applicable to vertically-modulated frequency records. The oldest of these is the "Microscope Method," in which the recorded amplitude is measured directly by use of a microscope.

The second method is the "Light-Pattern Method," in which the recorded amplitude is determined by use of the principle that, under specified conditions, the reflected light from a band of recorded grooves forms a pattern the width of which is related to the recorded velocity. The main body of the Standard covers the Light-Pattern Method due to Buchmann-Meyer, while in the Appendix are given two approved refinements for improving accuracy of observation, particularly at short-recorded wavelengths.

In the third method, the "Variable-Speed Method," a pickup stylus is engaged with the record groove and the record is rotated at different speeds. Thus, the pickup stylus is driven at a constant amplitude for a given recorded groove band, and the pickup output frequency is proportional to groove speed. By providing several bands with different recorded wavelengths on the record, and by operating over a sufficient speed range, an overlapping of the pickup output frequency from one band to another will result, and the response-frequency characteristics of the pickup itself can be factored out of the measurement of recorded amplitude.

No single standard method for calibrating mechanically-recorded frequency records yet devised gives completely accurate results under all conditions, particularly at high recorded frequencies. Accordingly, in recording and reproducing practice, all three basic methods described in this Standard are used in order to cross-check results and average out errors in measurement. The Microscope Method is limited in precision by the optical and mechanical properties of the available microscope and accessory equipment. Under optimum conditions recorded amplitudes as small as 50 micro-inches can be measured with less than 10 per cent error. This sets a practical upper frequency limit on the Microscope Method of about 10,000 cps for a recorded level of 5 cm per second. The basic Light-Pattern Method is limited in accuracy at both very low and very high frequencies, due to the diffuse nature of the pattern edges. Nevertheless, under proper conditions this method can provide reasonable accuracy at recorded frequencies as high as 15,000 cps, particularly with the refinements in technique described in the Appendix. The Variable-Speed Method is accurate through the lower and middle

ranges of frequencies, but suffers increasingly serious errors at high frequencies where the recorded wavelength is less than about 3 times the stylus radius.

2. MICROSCOPE METHOD OF MEASUREMENT

In the Microscope Method of Calibration the recorded grooves of a frequency record are viewed directly with a microscope having a magnifying power range between 25 \times and 500 \times , and arranged to provide vertical illumination of the grooves. Each frequency to be measured need be recorded for only a few cycles with suitable identification breaks between frequencies.

2.1 Measuring Equipment for Microscope Method

2.1.1 Apparatus: Any conventional microscope having a vertical illuminator may be used with the following typical apparatus:

Filar micrometer eyepiece having a magnification of about 12.5 \times .

Achromatic dry microscope objectives—48 mm, 32 mm, 16 mm, 8 mm, 4 mm, corrected for use without cover glass, and designed for tube lengths which match the microscope barrel lengths with the vertical illuminator in place. Ease of observation is materially increased if the glass surfaces of the objectives are treated with a reflection-reducing coating.

Mechanical stage.

Collimated light source with adjustable iris diaphragm.

Record fixture which will support the frequency record to be measured beneath the microscope objective.

Glass stage micrometer for calibrating the setup.

2.1.2 Arrangement of Apparatus: It is desirable that the measuring equipment be set up on a sturdy bench. The filar micrometer eyepiece is used to replace the regular microscope eyepiece and the vertical illuminator is mounted on the barrel of the microscope. The objective is fastened to the vertical illuminator and a source of collimated light placed opposite the light aperture of the illuminator at a distance of from 2 to 3 inches. The arrangement of this apparatus is shown in Fig. 1. It is essential that the iris diaphragm on the light source be closed down until optimum contrast and resolution of the image are obtained. The light source and the position of the mirror in the vertical illuminator should be adjusted until a small circular spot of light is projected onto the record.

2.2 Measuring Procedure for Microscope Method

2.2.1 Calibration of Microscope: The divisions of the filar micrometer eyepiece may be calibrated for each objective lens by placing the glass stage micrometer beneath each objective lens. In order to minimize measurement errors arising from the limiting accuracy of

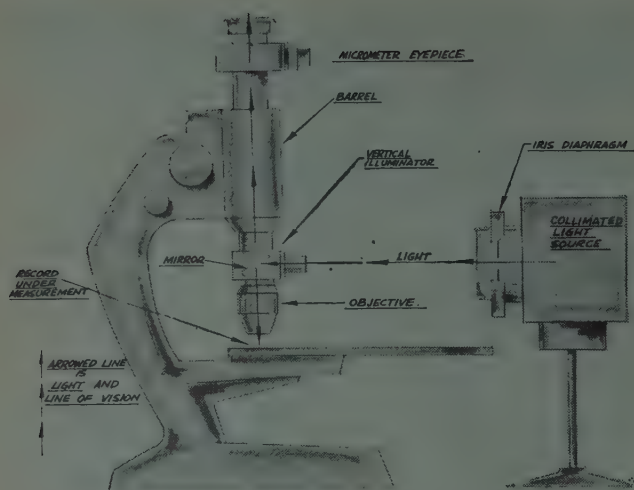


Fig. 1—Arrangement of apparatus for Microscope Method of calibrating mechanically-recorded frequency records.

calibration of the micrometer screw, it is important, particularly at high recorded frequencies, that the filar eyepiece be calibrated at that portion of the screw where the amplitude measurement is to be made. In use, that objective is chosen which will give a measurable image of the recorded groove modulation in the microscope eyepiece.

2.2.2 Measuring Technique: The record to be calibrated is supported on the fixture under the microscope as shown in Fig. 1. An objective should be chosen which gives a magnification sufficient to observe several wavelengths of the frequency band being measured. With the vertical illuminator adjusted as above, the groove edges or bottom will be defined by the reflected light, as shown in Fig. 2. The maximum excursions can be measured with the micrometer eyepiece. When high power objectives are used, it becomes apparent that the grooves are not perfectly smooth. Fine lines parallel to the groove bottom caused by stylus imperfections are frequently clearly visible and may also be used for the measurement of amplitude.

2.3 Results with Microscope Method

2.3.1 Limits of Accuracy: With this method it is possible, if the groove wall is sufficiently well defined and if the precision of the optical equipment is adequate, to make useful measurements of recorded frequencies as high as 10,000 cps. A 10,000-cps signal recorded with normal stylus velocity of 5 centimeters per second rms will have an amplitude of 88.7 micro-inches peak to peak.

2.3.2 Method of Presentation: The individual measured amplitudes may be tabulated or plotted directly as a function of the recorded frequency. It is customary in recording practice to use the term "decibel" to express the relative amplitude of each of the recorded frequencies. This is accomplished by multiplying by 20 the common logarithm of the ratio of each amplitude to the amplitude of a recorded reference frequency. For some work, stylus velocity may be desired, and this can be

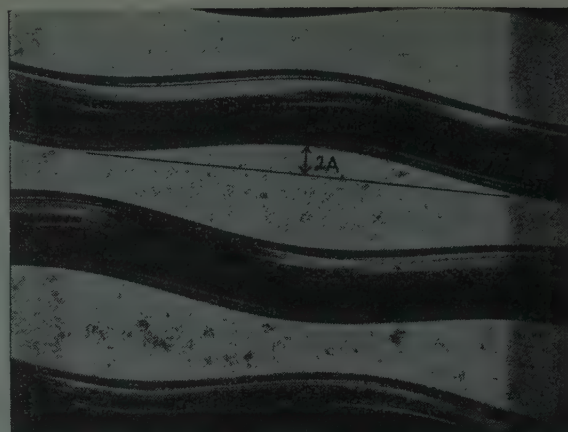


Fig. 2—Photograph showing typical recorded-groove section as observed by Microscope Method. Recorded frequency is 1000 cps, and magnification is 250 \times . Peak-to-peak recorded amplitude $2A$ is 0.00056 inch, corresponding to a velocity of 8.9 cm/sec.

readily calculated from the amplitude, by the relations

$$V_{\max} = 2\pi fA$$

or

$$V_{\text{rms}} = \sqrt{2}\pi fA,$$

where A is one half the peak-to-peak amplitude as measured, and f is the recorded frequency. The calculated velocity data may be tabulated or plotted either directly as a function of the recorded frequency, or as relative recorded velocity with respect to the velocity at a reference frequency. Relative recorded velocity is customarily expressed in decibels by multiplying by 20 the common logarithm of the ratio of the calculated velocity to the velocity of a recorded reference frequency.

3. LIGHT-PATTERN METHOD OF MEASUREMENT

A frequency record intended for calibration by the light-pattern method¹ is prepared by recording each frequency for a sufficiently long time to produce a band of at least ten modulated grooves. A similar number of unmodulated grooves is left between the modulated bands. The higher frequencies are usually recorded at the outside of the record, with frequencies decreasing toward the center.

3.1 Apparatus and Measuring Setup for Light-Pattern Method

A light approximating a collimated source is required. A point source may be used at sufficient distance. A clear-glass incandescent lamp with one straight-coil filament is adequate. A turntable support for the record is also needed, together with a scale graduated in centimeters. A suggested arrangement for making measurements by this method is shown in Fig. 3.

Also shown in Fig. 3 are detail sections illustrating the reflection of the light from the inner and outer groove walls to the viewing positions for taking bandwidth measurements. An optional refinement in technique

¹ G. Buchmann and E. Meyer, "Eine neue optische Messmethode für Grammophon platten," *Elek. Nachr.-Tech.*, vol. 7, p. 147; 1930. Translated in *J. Acoust. Soc. Amer.*, vol. 12, p. 303; 1940.

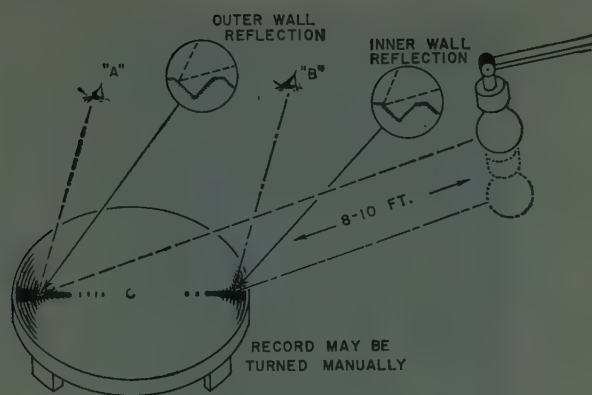


Fig. 3—Suggested arrangement of apparatus for Light-Pattern Method of calibrating disc records.

would substitute a telescope measurement for direct measurement with the scale. Still further refinements are obtained by the use of color filters and photography.

3.2 Measuring Procedure for Light-Pattern Method

The type of light pattern resulting from use of this method is indicated in Fig. 3. The widths of both inner and outer reflected light bands for each frequency are measured directly while observing from the position which gives the most brilliant pattern reflection. For low frequencies it is necessary to rotate the disk so that reflections at the outermost edges appear. Continuous rotation gives the best results at all frequencies.

The recorded velocities may be obtained by application of the following formula:²

$$V = 2\pi(N/60)(B_o B_i)/(B_o + B_i)$$

where

V = the maximum recorded velocity of modulation, cm. per sec.

N = revolutions per minute at which the record was recorded.

B_o = width of outer pattern in centimeters (pattern farther away from the light source).

B_i = width of inner pattern in centimeters (pattern nearer the light source).

3.3 Limitation of Light-Pattern Method

Measurements made by the light-pattern method described above are subject to the major limitation that the light pattern does not end abruptly at its sides, but rather exhibits a slow drop-off, providing a degree of uncertainty in the measurement of pattern width, especially at short recorded wavelengths. At long recorded wavelengths the pattern width is small, and accurate results are increasingly difficult to obtain. In addition, cyclic shifting of the pattern results from geometric inaccuracies in the disc, such as groove eccentricity and lack of disc flatness.

Two methods are described in the Appendix for improving the accuracy of measurements at short re-

corded wavelengths. The first method³ uses the principle of the sextant to provide improved accuracy of measurement. The second method⁴ makes use of interference patterns from which the theoretically correct pattern width can be calculated.

4. VARIABLE-SPEED METHOD OF MEASUREMENT

This method consists of reproducing the several frequency bands of the frequency test record under measurement with a conventional pickup and a variable-speed turntable. One of the recorded frequency bands on the frequency record is selected as a reference frequency band. The turntable speed is adjusted for each of the other frequency bands in turn, so that the reproduced frequency in each case is the same as that of the reference band.⁵ The pickup output voltage for each band is then compared with the reference frequency band pickup output voltage. By taking into account the relative output voltages and normal recorded frequencies, simple calculations can be made which give the relative recorded velocity of each band compared to the velocity level of the reference frequency band. When a wide range of frequencies is to be measured, more than one reference frequency band usually must be used to cover the entire range.

4.1 Measuring Equipment for Variable-Speed Method

A turntable, the speed of which is continuously variable over a range of the order of 10 or 15 to one, is required. The low-speed limit may typically be 5 to 10 rpm; the high-speed limit 80 to 100 rpm. A conventional tone arm and a high-compliance pickup with suitable stylus for the type of record to be calibrated is also required. Measuring equipment consists of a suitable vacuum-tube-voltmeter capable of measuring the pickup output voltage and, where necessary, suitable band-pass filters for attenuating record noise.

4.2 Measuring Procedure for Variable-Speed Method

Selection of the reference frequency bands will depend to some extent on the normal speed of the record to be calibrated and the speed range of the turntable. The first, or lowest, reference frequency band should be selected so that all of the low-frequency bands on the record up to approximately 200 cycles may be reproduced at this lowest reference frequency by either increasing or decreasing the turntable speed. The pickup output from each band when reproduced at the reference frequency should be noted and compared with the output from the reference frequency band when reproduced at normal speed for the record.

The above procedure should be repeated, using one or more higher reference frequencies selected so the group

² P. E. Axon and W. K. E. Geddes, "The calibration of disc recordings by light-pattern measurements," *Proc. IEE*, vol. 100, pt. III, pp. 217-227; July, 1953.

³ B. B. Bauer, "Calibration of test records by interference patterns," *J. Acoust. Soc. Amer.*, vol. 27, pp. 586-594; May, 1955.

⁵ R. C. Moyer, D. R. Andrews, and H. E. Roys, "Methods of calibrating frequency records," *Proc. IRE*, vol. 38, pp. 1306-1313; November, 1950.

² B. B. Bauer, "Measurement of recording characteristics by means of light patterns," *J. Acoust. Soc. Amer.*, vol. 8, p. 387; 1946.

of bands measured at each reference frequency will overlap by one or more bands those measured at the next lower reference frequency.

4.3 Results with Variable-Speed Method

The relative recorded velocity of each test frequency band in a group, compared to the recorded velocity of the reference frequency band, may be expressed as follows:

$$\text{Relative recorded velocity in db} = 20 \log \left[\frac{E_r f_x}{E_x f_r} \right]$$

where

E_r = voltage output from reference band.

E_x = voltage output from test band when reproduced at reference band frequency.

f_r = recorded frequency of reference band.

f_x = recorded frequency of test band.

Similar calculations may be made for each group of bands where a different reference band frequency is selected. Since overlapping groups of frequency bands have been selected, the various portions of the calibration curve thus arrived at may be arbitrarily connected at common frequency points, thereby producing a continuous calibration curve for the bands measured. Absolute velocity calibration in centimeters per second may then be obtained by determining the velocity of one band by either of the two preceding methods.

4.3.1 Limitations of Variable-Speed Method: For accurate results with the variable-speed method the stylus of the calibrating pickup must track the record grooves perfectly, and the record material must not yield either under the downward pressure of the stylus tip or as the groove walls apply vibratory movement to the stylus. However, at high velocities the resulting stylus accelerations cause forces of a sufficient degree to cause appreciable yielding of the material. (A correction formula⁶ has been developed to take such yielding into account.) The lower the mass of the pickup elements set in vibration by the stylus, the lower such forces will be. The higher the compliance of the pickup mechanism, the more perfect the tracking will be. Accordingly, the closer the approach to a zero-mass, zero-stiffness pickup, the more accurate the above results will be. Additionally, as velocities are reached which produce curvatures of the groove which are comparable to the stylus tip radius, the poorer the tracking will be. Thus, this method has limitations which generally become more marked, the higher the recorded frequency.

APPENDIX

The limitations of the basic Light-Pattern Method indicated in Part 3.3 may be reduced by the refinements in techniques presented in this Appendix.

⁶O. Kornei, "On the playback loss in the reproduction of phonograph records," *J. Soc. Mot. Pict. & Telev. Engs.*, vol. 37, pp. 569-590; December, 1941.

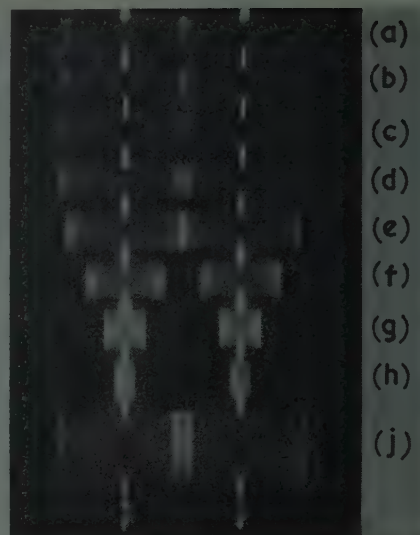


Fig. 4—Photograph of twin images formed by the sextant technique for making light-pattern measurements of disc records. Images are adjusted for coincidence of the 500-cps tone patterns.

Tone-Pattern Frequencies

(a) 4 kc	(d) 1 kc	(g) 100 cps
(b) 3 kc	(e) 500 cps	(h) 50 cps
(c) 2 kc	(f) 200 cps	(j) 1 kc

(Reprinted with permission from reference 3.)

A. SEXTANT TECHNIQUE FOR MAKING LIGHT-PATTERN MEASUREMENTS

This method of measuring the light pattern width uses the principle of the sextant. Two identical images of the light pattern are produced, and these images are moveable with respect to each other in a horizontal direction. The width of a light pattern corresponding to a given recorded frequency is measured by the relative displacement of the two images necessary to cause the right-hand edge of one to coincide with the left-hand edge of the other. This type of alignment is relatively unaffected by oscillation of the pattern, such as would result from groove eccentricity and lack of disc flatness, since both images move together in an identical manner. The type of pattern resulting from application of this technique is shown in Fig. 4, where the 500-cps patterns have been adjusted for edge-to-edge coincidence. Pattern width is measured by the center-to-center distance between the images for the coincident condition.

A.1 Apparatus and Measuring Procedure

A diagram of the measuring apparatus is shown in Fig. 5. Light from the lamp L_1 is reflected by the inclined plane mirror M_1 to the collimating mirror C . The collimated beam of light is limited in vertical extent by the slit S and passes above the prisms P_1 and P_2 , and between the mirrors M_1 and M_2 , to the disc. It can be shown that when the light source is at infinity (a condition approximated by the collimated light source), the focal plane of the light reflected from either the near-side or far-side grooves coincides with the vertical plane through the center of the disc. In the sextant method the reflected light pattern is viewed at its focal plane

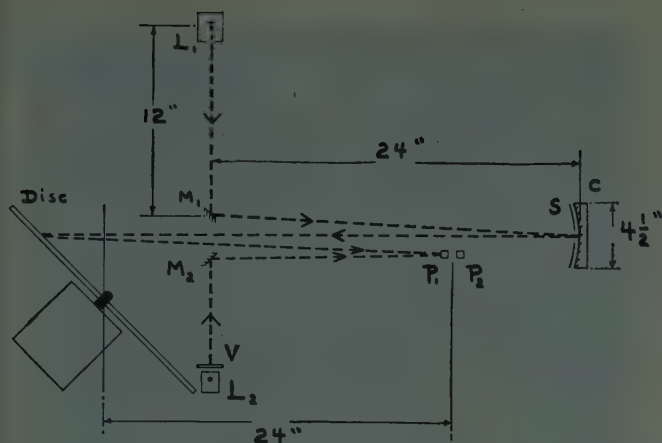


Fig. 5—Functional diagram showing arrangement of optical elements with the sextant technique for making light-pattern measurements. (Reprinted with permission from reference 3.)

rather than at the surface of the disc, so that by moving the disc vertically all patterns, whether near side or far side, are brought to the same point for observation.

The turntable is rotated at about 20 rpm, which is just sufficient to merge the luminous elements of a 50-cps band of tone into a continuous pattern.

The two separable images are produced respectively by the prisms P_1 and P_2 , which reflect the light from the disc through a right angle, in a direction normal to the plane of the diagram. When the prisms are parallel, as in the plan view shown in Fig. 6, coincident images of the light pattern are observed in the telescope, while counter-rotation of the prisms about a vertical axis causes the two images to separate horizontally. The linear movements of the images can be made equal and opposite if the prism P_1 , which is nearer to the pattern, is arranged to rotate slightly more rapidly than P_2 .

When a correct edge-to-edge adjustment has been made, the separation of the two images is equal to the width of the light pattern and is measured by observation of a vernier scale system, V (Fig. 5). To read the scale the lamp L_2 is switched on and an image of the scale is formed by the mirror M_2 in the focal plane below the light pattern but still within the field of view of the telescope. Twin images of both the scale and the light patterns will then be seen and their separation may be read off directly. The vernier is illuminated by light of one color and the main scale by another, appropriate color filters being inserted into the respective image paths via P_1 and P_2 . This allows the vernier to be seen moving across the scale without redundant and confusing duplicate images.

The vertical spread of the collimated beam due to the length of the filament of L_1 allows some latitude in the inclination of the disk necessary to secure adequate reflection into the viewing system. The width of the collimated beam is the limiting width of patterns which may be measured.

A.2 Results with Sextant Method

Results with the sextant technique show good corre-

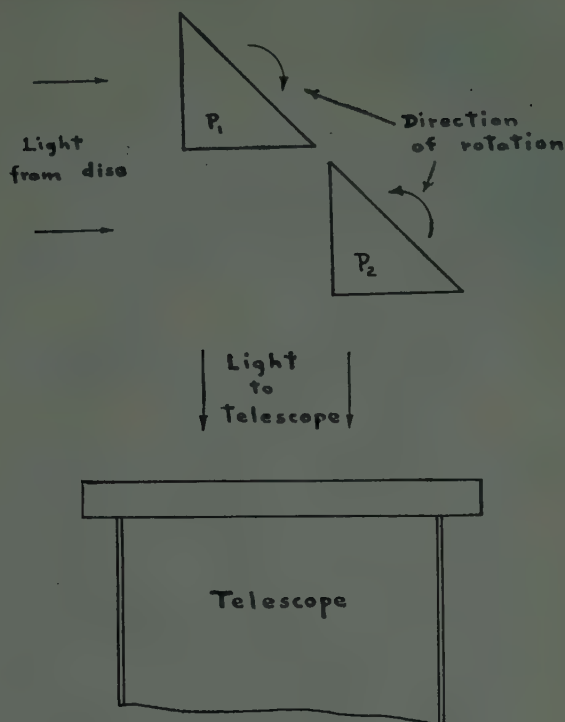


Fig. 6—Plan view showing arrangement of prism and telescope in the sextant technique for making light-pattern measurements. (Reprinted with permission from reference 3.)

spondence of velocity ratios determined from near-side pattern measurements with those from far-side measurements. The edge-to-edge adjustment is not affected by oscillation of the pattern which may result from lack of perfect flatness in the disc surface or by eccentricity and wobble of the disc during rotation. The sextant principle provides an improved means of gauging the edges of the reflected light pattern and increases the accuracy and repeatability of the measurements at all frequencies.

B. B-LINE LIGHT PATTERN METHOD OF MEASUREMENT

When a reflected light pattern from a test record is examined through appropriate color filters, two distinct interference patterns of lines appear. These lines have been designated by Bauer⁴ as A lines and B lines. The A lines are identified with the frequency and the B lines with the amplitude of the signal recorded on the test record. The B -line method is most suited for measuring recorded frequencies above 1000 cps.

B.1 Measuring Equipment and Setup

In addition to the apparatus required for the basic Light-Pattern Method, a color filter is required. In most instances a type "A" red photographic filter will be satisfactory. The arrangement of apparatus is shown in Fig. 7. An intense source of light is recommended, and this can conveniently take the form of a slide projector. Measurements may be performed visually by means of a ruler or a scale, as in Part 3.2. For maximum accuracy,

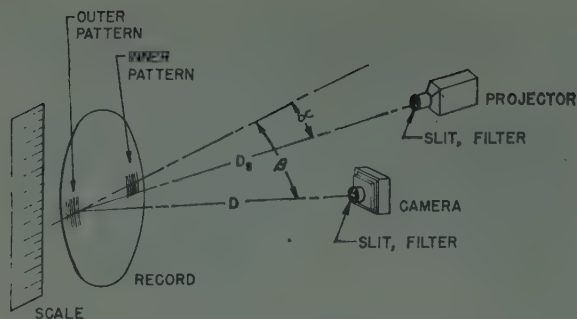


Fig. 7—Arrangement of apparatus for making light-pattern measurements by the *B*-line technique.

however, it is best to photograph the patterns. The camera lens should be provided with a slit having a width approximately $f/100$, where f is the focal length of the lens, to produce a sharp, well-defined pattern of the interference lines. The slit may be cut from opaque paper and inserted into the camera filter holder. If the light source is a projector, it should preferably also be provided with a slit having a width of approximately $D_s/100$, where D_s is the distance from the light source to the record. A scale should be placed near the pattern so that it will appear in the photograph and allow for ease of measurements.

B.2 Measuring Procedure for *B*-Line Method

It is recommended that the projector be placed at 6 feet or more from the record with the projector slit so oriented that it will be in the plane passing through the camera, the projector, and the pattern. The camera should be placed at about 2 feet or more from the record; the distance being determined by ability to focus clearly upon the grooves and the scale divisions. The angle α of Fig. 7 is preferably about 20° and the angle β will then be approximately $90^\circ - \alpha$, or 70° . With the filter and slit removed from the camera, angles α and β should be adjusted until a clear and bright pattern is reflected into the camera. After focusing, the slit and filter are installed in the camera and the camera slit is oriented so that it will be in the plane passing through the camera, the projector, and the pattern. The camera lens iris is preferably adjusted to $f:4.5$ or slower. It is recommended that a series of exposures variously timed be made to insure a properly exposed image. After one side of the pattern has been thus photographed, the record is moved in its own plane until the second pattern is in view and the above procedure is repeated.

B.3 Results with *B*-Line Method

Two types of interference patterns can be observed in the typical photograph of Fig. 8.

a) A set of evenly-spaced dark lines, independent of the amplitude of modulation, are dependent only upon frequency of modulation, the color of light, and the rotational speed at which the disc was recorded. These

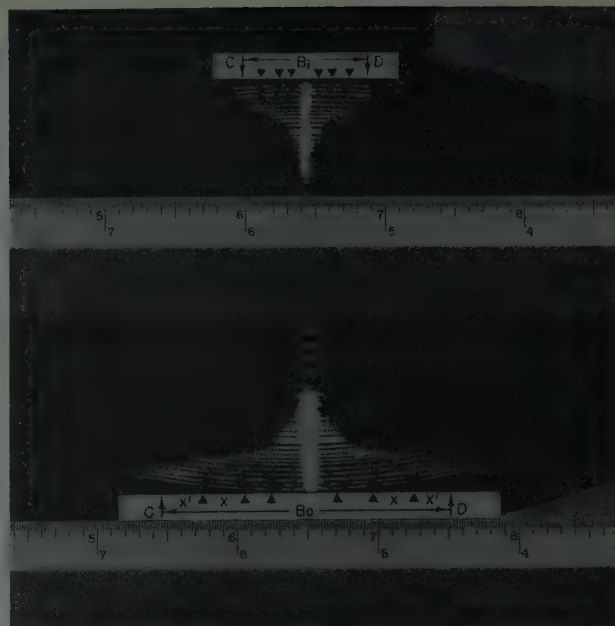


Fig. 8—Photograph of typical light pattern resulting with the *B*-line technique. *B*-lines are denoted by the black arrowheads, and the theoretical lengths of the light pattern for both the inner and outer reflections are shown by B_i and B_o , respectively.

are called the *A* lines and they are of no interest in record calibration.

b) The set of lines most clearly visible toward the sides of the pattern which are broader than *A* lines, are unevenly spaced and are dependent upon the amplitude of modulation. These are called *B* lines and they are useful in calibrating records. *B* lines are "modulated" by the *A* lines.

In accordance with the *B*-line pattern theory, the correct width of the pattern is obtained by adding to the outer *B* lines a measure equal to the distance between the first and second *B* lines. In Fig. 8 the distance between the first and second *B* lines, B_1 and B_2 , is labeled x . This distance is added on both sides as x' establishing the theoretical ends of the pattern at points *C* and *D*. The distance between these points, B_o , is the *B*-line width of the pattern. The solid triangles denote the positions of the *B* lines. B_o is the *B*-line pattern width for the outer pattern; B_i is the *B*-line pattern width for the inner pattern. The modulation velocity is found by the following equation:

$$V = 2\pi(N/60)(B_o B_i)/(B_o + B_i)$$

where

V = maximum velocity of modulation, cm per sec.

N = record speed, rpm.

B_o = *B*-line pattern width of the outer pattern, cm.

B_i = *B*-line pattern width of the inner pattern, cm.

This method is useful only for frequencies above 1000 cycles. Above this frequency it provides more sharply defined measuring points than the normally-viewed pattern edges with a resultant improvement in accuracy.

Correspondence

D-Day in Engineering Education*

At the risk of being called an old fogey (I am a 34-year-old graduate student), I should like to take issue with part of the editorial in "Poles and Zeros."¹

For the past several years I have observed young engineering graduates reporting for work in a government lab. These young men, of widely varying degrees of ability, all seem to have one trait in common. They are reluctant to work with their hands. The drawings they turn out are smudges. They approach a drill press with trepidation, and will go to any lengths to avoid a lathe. Few can wire a chassis with any dexterity.

But far more serious than lack of manual skills (which, after all, can be learned on the job) is the common attitude that manual work is "for technicians," and therefore is somehow beneath their dignity. As one of them proudly put it: "An engineer should only do theoretical work."

If, as I suspect, this attitude springs from the elimination of drafting and shop courses from the curricula of some schools, then I seriously question the wisdom of such removal. I submit that an engineer who avoids the practical aspects of his profession is less than half an engineer—he cannot command the respect of the technicians and artisans he will eventually be supervising, nor can he really appreciate the problems of construction and production of hardware; which, after all, is the ultimate purpose of engineering.

I am in no way trying to question the value of theory. By all means, let us have as much of basic physics and mathematics as we can cram into the curricula. But let us not forget that the mind is often at its best when the hands are occupied!

CHARLES E. HENDRIX
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Los Angeles 45, Calif.

Although I have many gray hairs, I am still struggling toward getting an education. I have some strong feelings about our education system, and the editorial in "Poles and Zeros" hits on my gripe. However, after reading it several times, I'm not sure how its writer stands.

My complaint about the education system is that too many redundant subjects are required to obtain an EE degree. For instance, I would like to take technical writing. The prerequisite for this course is 7 semesters (Georgia Tech) of "English." My investigations show that these "English" courses are not composition and rhetoric, but literature. I fail to see the bearing that literature has on technical writing. Likewise most colleges require languages and history. Granted, these subjects would be nice to

take if we had the time or desire to take them.

In my 20 years of work in industry I find many who agree with my stand. Many professional educators disagree. Aren't we being influenced too much by the "polished" white shirt educator and engineers and overlooking what we really need to know to beat Russia?

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Current Build-Up in Semiconductor Devices*

INTRODUCTION

The purpose of this letter is to lay a mathematical foundation for the switching action of devices in which carrier multiplication at a collector junction plays an important role in the switching process. The physical source of this multiplication may be an avalanche effect, hook-collector action, or a similar multiplicative mechanism. The mathematical formulation of the general problem will, of course, depend on device geometry as well as on operating conditions, so that in addition to predicting the functional dependence of switching time on multiplication, we may expect the results to provide important information concerning the efficacy of various possible design procedures whose aim is improved switching speed.

The analytical technique to be used is one that finds frequent use in the solution of partial differential equations and can be used to advantage in treating minority carriers in a semiconductor. We assume that during the switching action, minority carrier densities and the currents associated with them are increasing at an exponential rate in time. We then attempt to find a self-consistent solution to the equations governing the behavior of currents and carrier densities in the device.

Although the assumption of exponential build-up does not require mathematical justification, a physical interpretation may be helpful. Consider the three-layer diode shown in Fig. 1, and suppose one injects a delta function containing P holes across junction 1. These holes move across the n base layer and enter the depletion region at junction 2. We suppose for simplicity that the form and amplitude of the delta function are maintained throughout its motion across the base. Suppose further that in the depletion region each hole experiences an instantaneous multiplication, so that each hole from the base results in M holes at the col-

lector layer. Now each ionizing collision produces a hole-electron pair, and the direction of the depletion-layer field is such that the electrons so produced move into the base. Thus, a transfer of qMP units of charge across the depletion layer occurs.

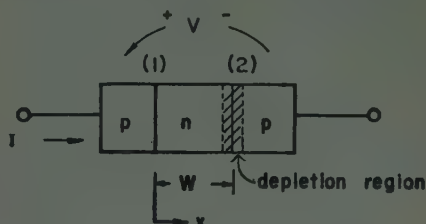


Fig. 1—Three-layer diode, or transistor with base bias lead not shown.

This charge is carried to the base by qP units of charge, which were brought in to neutralize the originally injected holes, and $q(M-1)P$ units due to secondary electrons. The effect of this increase of electrons into the base is to draw an additional charge of holes into the base at junction 1 to maintain space-charge neutrality. This added hole density is in the form of a delta function, its magnitude being M times the original delta function.

On a time scale, the amplified replica of the originally injected holes appears τ_0 seconds after the first one, where τ_0 is the transit time for holes across the base. The cycle of operations just described now repeats itself with this amplified input to form a geometrically increasing series.¹ The result of three such cycles is shown graphically in Fig. 2. The envelope of the injected hole density at junction 1 is seen to be exponential; the time constant is evidently a function of M and the device construction parameters. We anticipate this time dependence mathematically by assuming at the outset that $p(x, t) = p(x)e^{t/\lambda}$, and expect to find a functional relationship between λ and the device parameters.

Before proceeding with the program outlined, however, we note that the assumptions above would accurately depict the exponential build-up if the injected holes had an infinite lifetime and moved across the base by drift only in a constant field. For this slightly artificial but very instructive case, we may quickly arrive at the time constant as follows.

We note that

$$p(t + n\tau_0) = M^n p(t). \quad (1)$$

Therefore,

$$\ln [p(t + n\tau_0)/p(t)] = n \log M. \quad (2)$$

Now the value of $n\tau_0$ for which $p(t + n\tau_0)$ is just equal to e times $p(t)$ is by definition the time constant.

* Received by the IRE, May 26, 1958. This work was supported by Signal Corps contract. It was presented at the Congrès International de l'Etat Solide et ses Applications à l'Electronique et aux Telecommunications, Brussels, Belgium, June, 1958, and should appear in the report of the conference.

¹ Reasoning of this type has been previously employed by H. Statz and R. A. Pucel. "The spicitor, a new class of high-frequency semiconductor devices," Proc. IRE, vol. 45, pp. 317-324; March, 1957. See p. 322.

* Received by the IRE, September 18, 1958; and September 22, 1958.

¹ Proc. IRE, vol. 46, p. 1571; September, 1958.

Using (2), the value of n required is

$$n = [\log M]^{-1}$$

and therefore the time constant for the build-up is

$$\tau = n\tau_0 = \tau_0/[\log M]. \quad (3)$$

We return to this formula later for comparison purposes.

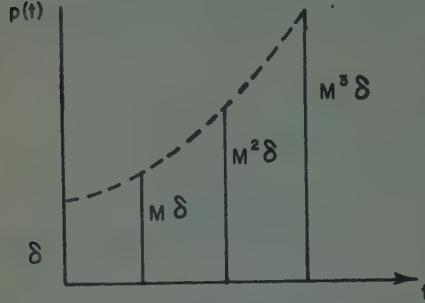


Fig. 2—Illustrating the build-up mechanism.

SOLUTION OF THE DIFFERENTIAL EQUATIONS FOR MINORITY CARRIER CONTINUITY

Proceeding now as outlined above, we write first the partial differential equation for hole continuity in the n base layer for the general case of hole motion by drift and diffusion:

$$\begin{aligned} \partial p / \partial t = & - (p - p_n) / \tau_p - p \mu_p \partial E / \partial x \\ & - \mu_p E \partial p / \partial x + D_p \partial^2 p / \partial x^2. \end{aligned} \quad (4)$$

We will first assume that holes move only by diffusion, so that (4) simplifies to

$$\partial p / \partial t = - (p - p_n) / \tau_p + D_p \partial^2 p / \partial x^2. \quad (5)$$

We now suppose that p consists of a dc part and an ac part

$$p = p_0(x) + e^{\lambda t} p_1(x)$$

so that the ac part of (5) becomes

$$\begin{aligned} \lambda p_1(x) e^{\lambda t} = & - [p_1(x) / \tau_p] e^{\lambda t} \\ & + D_p e^{\lambda t} d^2 p_1(x) / dx^2. \end{aligned} \quad (6)$$

Using the definitions

$$\begin{aligned} 1 / \tau_p = \nu_p \\ \xi = [(\lambda + \nu_p) / D_p]^{1/2} \end{aligned} \quad (7)$$

the solution to (6) can be written as

$$p_1(x) = A_1 e^{\xi x} + A_2 e^{-\xi x}. \quad (8)$$

We now assume that the switching is proceeding with a sufficiently large voltage across the device (this voltage appears as a back bias across junction 2) so that the hole density at $x=W$ can be set equal to zero. Mathematically,

$$p_1 = 0 \text{ at } x = W. \quad (9)$$

Using this in (8), we find the ratio of A_2 to A_1 and conclude

$$p_1(x) = 2A_1 \exp(\xi W) \sinh \xi(x - W). \quad (10)$$

Now the ratio of current carried by holes at $x=W$ and $x=0$ is

$$\begin{aligned} (\partial p / \partial x)_W / (\partial p / \partial x)_0 \\ = 1 / \cosh [W(\lambda + \nu_p) / D_p]^{1/2} = \beta(\lambda) \end{aligned} \quad (11)$$

where β is the transport factor for hole flow for the exponentially rising solution.

If γ is the injection efficiency at the emitter and $I \exp(\lambda t)$ is the total ac current through the device, then we may write

$$I \exp(\lambda t) = M \beta(\lambda) \gamma I \exp(\lambda t). \quad (12)$$

The right side of this equation is the total current crossing the collector junction. This current is M times the hole current arriving at the depletion layer, which in turn is $\beta(\lambda)\gamma$ times the total current at the emitter junction. Evidently $M\beta(\lambda)\gamma$ is the effective value of α for this case:

$$\alpha(\lambda) = M \beta(\lambda) \gamma. \quad (13)$$

Now, combining (11) and (12), we find

$$\gamma M = \cosh \xi W = \cosh [W(\lambda + \nu_p) / D_p]^{1/2}. \quad (14)$$

This equation contains only one unknown, λ . It therefore contains the functional relationship sought between λ and the device parameters. To obtain this relationship in a useful form, we first assume that $\nu_p = 0$ (infinite lifetime), and that $\gamma M > 3$. Then the error in approximating the cosh by a single exponential is less than 10 per cent and (14) becomes

$$\exp [W^2(\lambda / D_p)]^{1/2} = 2\gamma M.$$

Taking logarithms, we have

$$W[\lambda / D_p]^{1/2} = \log 2\gamma M. \quad (15)$$

Eq. (15) may be rewritten as

$$\lambda = D_p [\log 2\gamma M]^2 / W^2 \quad (16)$$

and the time constant associated with the build-up is thus

$$\begin{aligned} \tau = [\lambda]^{-1} = W^2 / D_p [\log 2\gamma M]^2 \\ = \tau_d / [\log 2\gamma M]^2 \end{aligned} \quad (17)$$

where τ_d is the diffusion time across the base layer.

Several interesting conclusions can be drawn with the aid of (17). Before doing this, however, we first make two observations.

First, by a process entirely similar to that just carried out, one may solve (4) under the assumptions that $D_p = 0$ and $\partial E / \partial x = 0$; i.e., carriers move only by drift in a constant field. Such a situation does not give a boundary condition of $p=0$ at $x=W$ and the appropriate solution is

$$p_1(x) = A \exp(\lambda + \nu_p)(W - x) / \mu_p E. \quad (18)$$

Eq. (13) still applies and gives

$$\gamma M = \exp(\lambda + \nu_p) W / \mu_p E. \quad (19)$$

Taking logarithms again and letting $\nu_p = 0$, find

$$\tau = \tau_0 / \log \gamma M$$

which reproduces (3) obtained earlier if we let $\gamma = 1$, as we did implicitly in the earlier derivation. τ_0 is once again the transit time, this time defined by $\tau_0 = W / \mu_p E$.

Our second observation is that if we let $M=1$ and $\lambda = j\omega$, (13) is identical to the expression normally obtained for alpha, which

is a result that one might anticipate. It is interesting to note this agreement, since no statement of boundary conditions on hole density at junction 1, the emitter, has been made. This of course points up the fact that the evaluation of β is a transport problem, not a junction effect.

We now return to (17) to see what suggestions it contains for the design of high-speed devices. As we should expect, τ depends directly on τ_d , and hence directly on W^2 . Therefore, other things being equal, decreasing the base width makes for a faster switching device. However, (17) also indicates that τ is a rather sensitive function of M , and may be decreased appreciably if M is great enough. This basic dependence of build-up speed on M is responsible in part for the generation of "millimicrosecond" pulses in transistors where the alpha cut-off frequency is much lower than the frequencies corresponding to $[\lambda]^{-1}$. [It also frequently happens that "punch-through" plays an important role in the pulse generators mentioned. This may be simply accounted for in (17) by noting that the base width modulation which finally produces the punch-through merely decreases the transit time τ_d .]

An instructive way to visualize the effects of multiplication in increasing build-up speed is to calculate the effective base width W^* during the switching, where W^* is defined by

$$\begin{aligned} W^* = W / \ln 2M\gamma \\ = W / [0.7 + \ln \gamma + \ln M]. \end{aligned} \quad (20)$$

Eq. (17) then becomes

$$\tau = (W^*)^2 / D_p \quad (21)$$

so that W^* is seen to be the base width which the device seems to have on a strictly diffusion basis. For most cases, γ will be nearly unity and $\ln \gamma$ will be negligible. Thus, for the following values of M , the reduction of W and increase of λ are given by the factors indicated in Table I. It should be noted that λ increases most rapidly for the smaller M 's.

TABLE I

M	10	100	1000	10,000
W^*/W	0.33	0.19	0.132	0.101
increase of λ	9	28	57	98

These values once again show the advantage of obtaining speed by using multiplication. Alternately, Table I indicates that a 100-mc transistor with no collector multiplication is roughly equivalent to a 3-mc transistor with a multiplication of 100 as far as build-up speed is concerned.

As a concluding observation, we note that there is a rather appreciable difference in the dependence of (3) and (17) on M . Eq. (3), which is the time constant for our hypothetical device where minority carriers move by drift only in a constant field, shows a $[\log M]^{-1}$ dependence, while (17), the time constant for the device in which minority carriers move only by diffusion, shows a $[\log 2M\gamma]^{-2}$ dependence. To explain this difference, we recall that when the minority carriers do move by diffusion, even though

the average particle takes a time τ_d to diffuse across the base, some of the particles arrive at the collector much faster than this. If the multiplication is high, these "early" particles may in fact entirely determine the resulting time constant. For motion in a field, however, there is no "spreading" of this sort; the form of the injected charge distribution is maintained throughout the transit and the average base transit time is the significant one. The conclusion to be drawn from these remarks is that if M is high, the time constant in the build-up will be determined predominantly by diffusion effects, even in graded-base devices.

The problem of voltage build-up is more complicated than that of current build-up considered here, because the variation of M with voltage and time leads to nonlinear integral equations rather than linear differential equations. The authors plan to submit results of a study of this problem in the near future.

An important generalization of (14) may be made by assuming that an admittance $A(\lambda)$ rather than constant voltage is applied between emitter and collector. We let $A_c(\lambda)$ represent the internal admittance of the collector junction where

$$A_c(\lambda) = \lambda C_c + r_c^{-1} \quad (22)$$

where C_c is the collector depletion layer capacity and

$$r_c^{-1} = (M - 1)nI_c/V_c \quad (23)$$

where I_c is the dc collector current and M is approximated by the conventional expression

$$M = [1 - (V_c/V_B)^n]^{-1} \quad (24)$$

Assuming that the admittance of the emitter junction is much larger than that of the collector, i.e., $qV_c/kT \gg (M-1)n$, we obtain in place of (14)

$$A(\lambda) [A(\lambda) + A_c(\lambda)]^{-1} \gamma(\lambda) \beta(\lambda) M = 1 \quad (25)$$

where the dependence of $\gamma(\lambda)$ allows for the variation of emitter efficiency with λ due to effective thinning [as in (20)] of the base layer for rapidly rising currents. If only capacitive terms are important, (25) shows that the larger the external capacitance, the faster the build-up, a result also obtained from the large signal theory.

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On the Need for Revision in Transistor Terminology and Notation*

Recently the writer has been conducting a course in transistor electronics. Whatever effect it may have had on the student, the experience has convinced him that the

terminology and notation need revision in order to get more nearly in step with things as they are, and that such a revision could make life a little easier, for the student at least.

Consider first the matter of configuration. It seems certain that most transistors are and will be used in the common-emitter configuration. Accordingly, that configuration should be taken as the standard, just as the common cathode is for vacuum tubes. Then the current gain figure, for example, should be the beta figure, and the alpha figure would not call for separate mention, any more than does the $\mu+1$ figure for the gain of a common-grid triode. The impression, incidentally, which one sometimes encounters, that the common-base configuration of a transistor is somehow more "fundamental" than the others, is, of course, without foundation. It is sometimes said, for instance, that the common-emitter transistor shows a larger current gain (and lower frequency possibilities) than does the common-base because it has positive feedback, as expressed by $\beta = \alpha/(1 - \alpha)$. But it is just as correct, and just as "fundamental," to say that the common base transistor has lower current gain and better frequency response because of negative feedback, as expressed by $\alpha = \beta/(1 + \beta)$. This latter way of looking at the matter, incidentally, might make the analogy between transistor and vacuum triode clearer. The high-frequency cutoff, of course, should refer to the common-emitter connection.

Thus the common-emitter current gain is of great importance. It has been designated β , or h_{21} , or h_{21e} , or h_{fe} , or in various other ways. The writer recommends that one symbol, not needing any subscripts, be used for it. Then subscripts could be reserved to indicate various stages, conditions, etc. Since the symbol β has already had some use, it would seem to be a logical choice.

Other quantities of interest are the input and output impedances. The common way of designating these, the output impedance for open input and the input impedance for shorted output, is desirable, since this corresponds most closely to the way in which the transistor will be actually used. Whether impedance or admittance values are quoted is rather unimportant. Thus the parameters h_{11} and h_{22} are suitable; perhaps, in order to use as few subscripts as possible, the symbols h_i and h_o , which are used sometimes, might be desirable. Another possibility would be to use the symbols y_i (input admittance with output shorted) and z_o (output impedance with input open); these definitions would agree with those which the symbols would have as elements of Y and Z matrices.

The symbol μ for the collector-to-base voltage feedback factor is diametrically opposite to the usage for the vacuum triode. Actually, this collector-to-base feedback factor should be considered as a "Durchgriff" or reciprocal of an amplification factor.¹ In many circuits, however, this quantity is of small importance anyway.

In the writer's opinion, the utility of the

h parameters, considered as matrix elements, and h matrix, in transistor circuitry, is greatly overrated. Often the statement is made that, because of the reaction of output on input, simple methods of analysis are unsuitable, and a matrix treatment should be used. Then, once that is granted, that is the last seen of matrix analysis, and the design proceeds by individual stages, the effects of reaction of output on input being taken into account through successive approximations, if necessary. Actually, if matrix methods are to be used in dealing with cascaded structures, the useful matrix is not the "hybrid" but rather the transmission matrix² (or transfer, or "chain," or "Kettenmatrix"). It is true that the hybrid matrix can have some utility in treating neutralization. From this viewpoint, if a matrix is to be quoted for the transistor, the transmission matrix would seem to be the useful one. The argument that the h matrix is used because its elements are readily measured is surely not valid; it is worthwhile to measure that set of values, but then, for quotation, to convert them to whatever set will be most immediately useful to the user.

Another quantity which seems rather illogical is the quantity I_{ceo} , the collector to base leakage current with open emitter. This quantity, or something related to it, is of great interest, especially as a function of temperature; but it is suggested that the collector leakage current with open base, possibly designated I_{co} , is a more immediately useful representation.

In the representation of characteristic curves, one still occasionally sees the voltage axis vertical and the current horizontal. It would seem worthwhile always to have the voltage axis horizontal and the current vertical, and, moreover, always to use the first quadrant; negative values, when required by the type of transistor concerned, would be indicated merely by signs. Incidentally, it would sometimes be very helpful if, in a plot of transistor output characteristics, e.g., an enlarged inset of the region within, say, 100 μ amp and 0.5 volt or so, of the origin, could be included, since this region of operation may be desirable for low noise.³

It is apparent that many of these anomalies in the terminology and notation are legacies from the point-contact transistor. In retrospect, one might say that the terminology and notation tried to develop more quickly than the device, and, accordingly, now find themselves not entirely suitable. Similar arguments have been presented concerning the graphical symbols,⁴ but it is not desirable to discuss that matter here. This should be an illustration, though, of the fact that it may be undesirable to try to standardize these things too quickly in a new field, lest the field later find itself saddled with a fossil notation and terminology.

* H. L. Armstrong, "A treatment of cascaded active four-terminal networks, with application to transistor circuits," IRE TRANS. ON CIRCUIT THEORY, vol. CT-3, pp. 138-140; June, 1956.

³ W. K. Volkers and N. E. Pedersen, "The hushed transistor amplifier," Tele-Tech and Electronic Indus., vol. 14, p. 82; December, 1955; vol. 15, p. 70; January, 1956; and p. 72; February, 1956.

⁴ H. E. Tompkins, "Foreword to transistor papers," IRE TRANS. ON CIRCUIT THEORY, vol. CT-4, p. 173; September, 1957.

¹ E. Benz, "Einführung in die Funktechnik," Springer Verlag, Vienna, Austria, 4th ed., p. 209; 1950.

In conclusion, this calls to mind one more point, which is connected with semiconductors, if not directly with transistors. When, oh when, will someone, in a definition, etc., dealing with Hall and related magnetic effects, admit that the field involved is the B field, not the H ?

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Antipodal Reception of Sputnik III*

The reception of radio signals from an orbiting earth satellite near the antipodes has been reported by Wells.¹ His observations have indicated that "in all respects, the image signals appeared to originate in a point source similar to the actual satellite."

The 20-mc radio transmissions from Sputnik III have been monitored by members of the Stanford University Radio Propagation Laboratory in an attempt to confirm this phenomenon. The signals were received on a standard communications receiver connected either to a fixed "turnstile" antenna $\frac{3}{8} \lambda$ above the ground, or to a three-element horizontal Yagi $\frac{5}{8} \lambda$ above the ground. The Yagi antenna can be rotated to determine the approximate direction of arrival of the signals. During most of the period means were available to determine the absolute frequency of the signals, and (when they were sufficiently strong to record them on magnetic tape.

Between May 16 and June 13, 1958, the high passages of Sputnik III near Stanford occurred in the afternoon or evening. On 13 occasions during this period signals from the satellite were observed at a time midway between two direct afternoon passes. In this same interval five attempts to receive these signals were unsuccessful, and two have been classified as questionable. The height of the satellite was approximately 1100 km when at the antipodes, and 800 km when at the receiving location. A plot of the afternoon data, similar to that given by Wells, is shown in Fig. 1.

The low passages of the satellite took place during the morning hours in this period. Antipodal signals were detected only twice, while 13 attempts were unsuccessful and two questionable. The antipodal height was near the apogee value of approximately 1800 km, and the height when executing a direct pass was about 220 km during these observations.

When the antipodal signals were observed in the afternoon on the Yagi antenna, the directions of arrival on all occasions were estimated to lie between southeast and southwest. On the assumption of normal earth-ionosphere multi-hop propagation, it

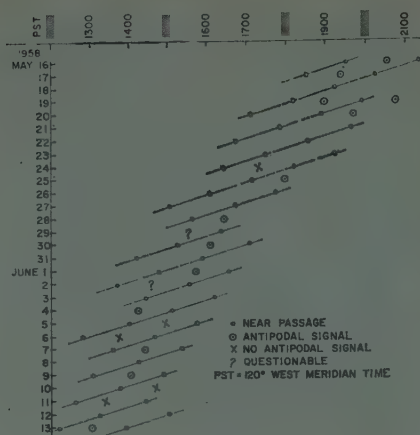


Fig. 1—Afternoon observations of the 20-mc transmissions from Sputnik III between May 16 and June 13, 1958.

is possible to estimate the direction of arrival of a signal by noting the amount of Doppler shift which has been imparted to it. Maximum positive shift should be observed in the direction in which the satellite will next approach for a direct passage. Maximum negative shift should be found in the direction in which the satellite last departed; intermediate shifts should be found in the intermediate directions. The absolute frequencies of the afternoon antipodal signals indicated Doppler shifts which were consistent with azimuths of arrival between southeast and south. The directions of arrival for the morning observations are not certain.

Perhaps the most significant signal characteristic was a nearly constant frequency throughout each antipodal passage. This requires that the arriving energy be confined to a relatively narrow cone in some unchanging direction. Fig. 2 is a spectrograph of the recorded signals during one of the strongest antipodal passages observed. If the signals had arrived simultaneously from several directions or throughout a wide cone, the observed spectrum would have consisted of several traces at different frequencies, or a single broad trace. If the direction of arrival had changed appreciably during the course of a passage, a corresponding variation in Doppler shift would have been observed.

On 53 occasions between June 14 and August 27 attempts to receive antipodal signals were unsuccessful. By the end of August the high passes of Sputnik III again occurred in the early evening and on August 28, signals were received from the southeast when the satellite was near the antipodes. A spectrum analysis of these signals shows several traces indicative of multipath propagation (Fig. 3). The presence of these components gives the signal a "rough" tone quality when monitored aurally, an effect which had not been noted previously. Antipodal signals have been observed on four occasions since then, up to the time of this writing (September 20, 1958).

The mode of propagation appears to involve penetration of the F layer followed by internal ionospheric reflection. The direction of arrival remains unchanged throughout each antipodal passage. The times of the observations suggest that the ionospheric tilt

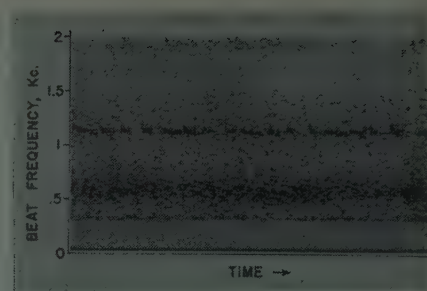


Fig. 2—Spectrum analysis of the signals received from Sputnik III while it was in the vicinity of the antipodes. This 5.6 second sample was recorded at 2046 PST, May 19, 1958, and the characteristic keying pattern is clearly visible a little above 1.1 kc. The absolute frequency was not determined on this passage.

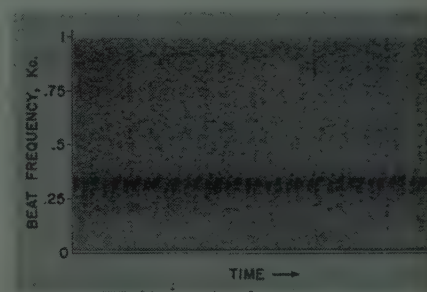


Fig. 3—Spectrum analysis of the signals from Sputnik III when it was close to the antipodes. This 11.2 second sample was recorded at 1815 PST, August 28, 1958. The detected signals are seen to be composed of several frequency components all near 300 cps. Absolute frequency = $20.004660 \pm$ beat frequency (mc). Knowledge of the direction of arrival (SE) and the approximate satellite oscillator frequency suggests the choice of the negative sign in this case.

to the southeast of the receiving location which occurs prior to local sunset is important in providing a propagation path and for selecting a narrow azimuth of arrival.

The assistance of D. M. Annett, whose efforts are responsible for much of the construction and operation of the receiving installation, is gratefully acknowledged.

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WWV Standard Frequency Transmissions*

Since October 9, 1957, the National Bureau of Standards radio stations WWV and WWVH have been maintained as constant as possible with respect to atomic frequency standards maintained and operated by the Boulder Laboratories, National Bureau of Standards. On October 9, 1957, the USA Frequency Standard was 1.4 parts in 10^9 high with respect to the frequency derived from the UT 2 second (provisional value) as determined by the U. S. Naval Observatory. The atomic frequency standards remain con-

* Received by the IRE, October 14, 1958.

* Received by the IRE, September 29, 1958. This work has been supported by grant no Y/32.43/268 from the National Science Foundation.

¹ H. W. Wells, "Unusual propagation at 40 mc from the USSR satellite," Proc. IRE, vol. 46, p. 610; March, 1958.

stant and are known to be constant to 1 part in 10^9 or better. The broadcast frequency can be further corrected with respect to the USA Frequency Standard as indicated in the table below. This correction is *not* with respect to the current value of frequency based on UT 2. A minus sign indicates that the broadcast frequency was low.

The WWV and WWVH time signals are synchronized; however, they may gradually depart from UT 2 (mean solar time corrected for polar variation and annual fluctuation in the rotation of the earth). Corrections are determined and published by the U. S. Naval Observatory.

WWV and WWVH time signals are maintained in close agreement with UT 2 by making step adjustments in time of precisely plus or minus 20 milliseconds on Wednesdays at 1900 UT when necessary; no step adjustment was made at WWV and WWVH during this month.

WWV FREQUENCY*	
September, 1958	Parts in 10^9
1500 UT	
1	-2.6
2	-2.7
3	-2.7
4	-2.7
5	-2.7
6	-2.8
7	-2.8
8	-2.8
9	-2.9
10	-3.0
11	-3.0
12	-3.0
13	-3.0
14	-3.0
15	-3.0
16	-2.9
17	-2.9
18	-2.8
19	-2.8
20	-2.6
21	-2.5
22	-2.4
23	-2.4
24	-2.4
25	-2.4
26	-2.4
27	-2.4
28	-2.4
29	-2.4
30	-2.4

* WWVH frequency is synchronized with that of WWV.

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Compound Interferometers*

The very interesting article by Covington and Broten¹ on a "compound interferometer" prompts the suggestion of another way of tackling the design of such systems. For simplicity, suppose that the system is a combination of a large number of elementary detectors, all similar and having little

or no directionality as individuals. The arguments can readily be extended to include continuous systems.

With this simplification, the system described by Covington and Broten resembles in form the system shown in Fig. 1. The over-all length contains $4n$ equally spaced positions. The unoccupied positions are marked with dots. Full circles show the two antennas of the simple interferometer. Asterisks show the numerous equally-spaced elements representing the continuous slotted-waveguide array. The distances of these elements from that on the extreme left are shown in the diagram as multiples of the basic interval D .

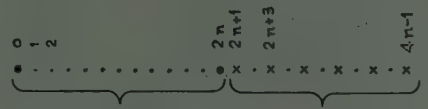


Fig. 1.

If u_r denotes the fluctuating electrical signal obtained from the detector that lies at a distance rD from the left, the signal from the simple interferometer is

$$U_1 = u_0 + u_{2n}$$

and the signal from the long array is

$$U_2 = u_{2n+1} + u_{2n+3} + \dots + u_{4n-1}.$$

Covington and Broten measure, in effect, the mean product of the signals U_1 and U_2 and this may be written, through the above equations, as the sum of many mean products of pairs of signals, one signal from a detector in the interferometer and one signal from a detector in the long array.

$$\begin{aligned} \overline{U_1 U_2} &= \overline{u_0 u_{2n+1}} + \overline{u_0 u_{2n+3}} + \dots + \overline{u_{2n} u_{2n+1}} + \dots \end{aligned}$$

The reception pattern appropriate to $\overline{U_1 U_2}$ is therefore the sum of reception patterns appropriate to these various pairs of elementary detectors. It can be shown that these elementary reception patterns are in fact sinusoids whose "space frequencies" are proportional to the distances separating the detectors in each pair. Thus, if the radio wavelength is L and the distance separating the detectors is $(2r-1)D$, then the reception pattern corresponding to the mean product of the signals of the two detectors is

$$\cos 2\pi(2r-1)D\theta/L \quad (1)$$

where θ is the angle of incidence (understood to be small).

It will be observed that in the arrangement of Fig. 1 the various pairs of detectors present every odd multiple of the basic distance, from D to $(4n-1)D$ and that each multiple appears only once. Thus the detector at $2n$ combined with the various detectors of the long array gives intervals $1, 3, 5 \dots (2n-1)$, times the basic distance. The detector at position 0 combined with the various detectors of the long array gives intervals of $(2n+1)$ to $(4n-1)$ times the basic distance D . Thus the reception pattern corresponding to $\overline{U_1 U_2}$ is

$$\begin{aligned} A(\theta) &= \sum_{r=1}^{2n+1} \cos 2\pi(2r-1)D\theta/L \\ &= \frac{\sin 4n(2\pi D\theta/L)}{2 \sin (2\pi D\theta/L)} \end{aligned} \quad (2)$$

This pattern has the optimum form discussed by Covington and Broten.

The same pattern could be obtained with other arrangements. Some of them are pictured in Fig. 2.

Fig. 2(a) and 2(b) have been described by Covington and Broten. In Fig. 2(c) and 2(d) the long array is reduced to one-third or to one-fourth of the over-all length of the system, and the simple interferometer is replaced by an array of three or of four detectors.

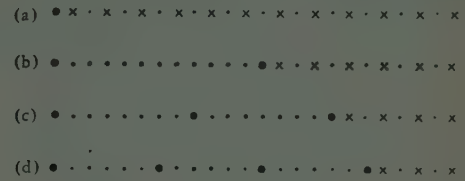


Fig. 2.

These systems all have the same reception pattern (2) because they all show the same set of space intervals between members of the two arrays.

It will be noted that Fig. 2(c) and 2(d) comprise only seven detectors while Fig. 2(b) needs eight and Fig. 2(a) needs thirteen. This economy in detectors could be of use in experiments where the individual detectors are costly. A system with a given over-all length uses the fewest detectors when the number of detectors in the two arrays are equal, or differ by unity.

The same test can be extended to two-dimensional arrays.^{2,3} Thus it is shown⁴ that the Mills cross has an optimum reception pattern in two dimensions, but that one of the four arms of the cross is redundant and can be omitted without affecting the performance.

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Authors' Comment⁵

We are pleased to see the interesting exposition and design for compound interferometers proposed by Barber, and would like to report that the original 300-foot compound interferometer in operation at the National Research Council's laboratories in Ottawa has now been doubled in length. This newer system may be explained readily with reference to the configurations shown in

² B. V. Mills, A. G. Little, K. V. Sheridan, and O. B. Slee, "A high resolution radio telescope for use at 3.5 m," Proc. IRE, vol. 46, pp. 67-84; January, 1958.

³ W. N. Christiansen and D. S. Mathewson, "Scanning the sun with a highly directional array," Proc. IRE, vol. 46, pp. 127-131; January, 1958.

⁴ N. F. Barber, "Optimum arrays for direction finding," N.Z.J. Sci., vol. 1, pp. 35-51; March, 1958.

⁵ Received by the IRE, July 7, 1958.

* Received by the IRE, May 16, 1958.
¹ A. E. Covington and N. W. Broten, "An interferometer for radio astronomy with a single-lobed radiation pattern," IRE TRANS. ON ANTENNAS AND PROPAGATION, vol. AP-5, pp. 247-255; July, 1957.

A simple, one-dimensional analysis may be made by representing the potential as

$$V(x) = \frac{zq^2}{\sqrt{x^2 + a^2}}, \quad a = \frac{L}{2} \quad (1)$$

where zq is the net capacitive charge of the aperture with L its cross-sectional dimension. Thus the barrier height is $2zq^2/L$. A critical trapping velocity v_c given by

$$v_c^2 = \frac{2zq^2}{m\sqrt{x_0^2 + a^2}} \quad (2)$$

defines the injection velocity v_0 for which an oscillatory motion arises; for $v_0 < v_c$, the potential barrier prevents the escape of the entering electron. In (2), m is the electron mass and x_0 the accelerative path length from cathode to aperture.

The amplitude and period of the oscillating, trapped electron have been characterized. The former has the values

$$x^* = \frac{\pm \sqrt{\frac{4z^2q^2}{m^2} - a^2 \left(v_0^2 - \frac{2zq^2}{m\sqrt{x_0^2 + a^2}} \right)^2}}{v_0^2 - \frac{2zq^2}{m\sqrt{x_0^2 + a^2}}} \quad (3)$$

The oscillation turns out to be nonlinear with the resultant power series development for the period T :

$$T = \frac{4(x_0^2 + a^2)^{3/4}}{\left(\frac{zq^2}{2m} \right)^{1/2}} \cdot \left\{ 1 + \frac{1}{12} - \frac{1}{4 \left(1 + \frac{a^2}{x_0^2} \right)} + \dots \right\} \quad (4)$$

Eq. (4) actually holds for the limit of $v_0 \rightarrow 0$; the general expression has been derived, but will be dealt with when a fuller discussion is presented at a later time. Nevertheless, it is clear from (4) that high-frequency oscillations associate with small dimensions and high voltages.

The classical, nonrelativistic theory pursued so far is adhered to in the determination of the radiated power per electron. The accelerative relation

$$a(x) = \frac{zq^2}{m} \frac{x}{(x^2 + a^2)^{3/2}} \quad (5)$$

employed in the power equation $P = dE/dt = (2q^2/3c^3)\alpha^2$ leads to the average radiated power

$$P_{av} = \frac{z^2q^5}{6c^3m^2} \left\{ \frac{1}{x^*} \cdot \frac{1}{2a^3} \tan^{-1} \frac{x^*}{a} + \frac{1}{2a^2} \frac{1}{x^{*2} + a^2} - \frac{1}{(x^{*2} + a^2)^2} \right\} \quad (6)$$

A complete understanding of the theoretical implications of the potential well theory of velocity modulation necessitates numerical evaluation of (3), (4), and (6). The interrelation of radiated power and frequency with dimensions and applied voltages will be quite interesting to elucidate in some detail. It is hoped that a deeper understanding of klystron operation may result from further study.

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Parallel Plane Waveguide Partially Filled with a Dielectric*

In a recent letter, Duncan *et al.*,¹ gave a qualitative description for a field configuration in a parallel plane waveguide partially filled with a dielectric. A more exact analysis, however, yields results which partially contradict the field structure picture presented in their letter.

Some of the principal points in the solution of this propagation problem and the final results for TE modes on this line are presented below. The geometry and coordinate systems are shown in Fig. 1.

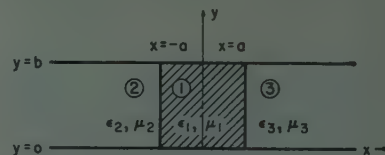


Fig. 1—Cross section of the parallel plane waveguide partially filled with a dielectric. The positive z axis is out of the paper.

The general solution of the scalar wave equation for TE modes is that

$$H_z = (Ae^{k_x x} + Be^{-k_x x})(Ce^{k_y y} + De^{-k_y y})e^{-j\beta z} \quad (1)$$

where

$A, B, C,$ and D are arbitrary constants,
 β = propagation constant,
 k_x and k_y are separation constants which come from the solution of the wave equation.

The separation constants k_x and k_y are related to the propagation constant, frequency, and properties of the medium by

$$k_x^2 + k_y^2 = \beta^2 - \omega^2\mu\epsilon. \quad (2)$$

The other field quantities can be obtained from the expression for H_z , and they are of similar form. Equations which are identical to (1) and (2) can be written for each of the three regions. Subscripts 1, 2, and 3 must be attached to each of the field quantities, arbitrary constants, material constants, and k 's to denote their respective regions. Of course, β must be the same for all three regions. Upon applying the boundary conditions at the conducting planes ($y=0$ and $y=b$), it is determined that

$$k_y = j \frac{n\pi}{b} \quad n = 0, 1, 2, \dots \quad (3)$$

It is assumed that $\mu_1 = \mu_2 = \mu_3 = \mu_0$, and $\epsilon_2 = \epsilon_3$. This symmetry of the structure causes all solutions to fall into two groups, even and odd modes. The distinction is based upon whether

$$E_y(x) = E_y(-x) \text{ or } E_y(x) = -E_y(-x). \quad (4)$$

When the proper boundary conditions are applied at one of the dielectric-air interfaces, it is found that if $n \neq 0$, a TE mode can propagate only if the entire space between the conducting planes is filled with a

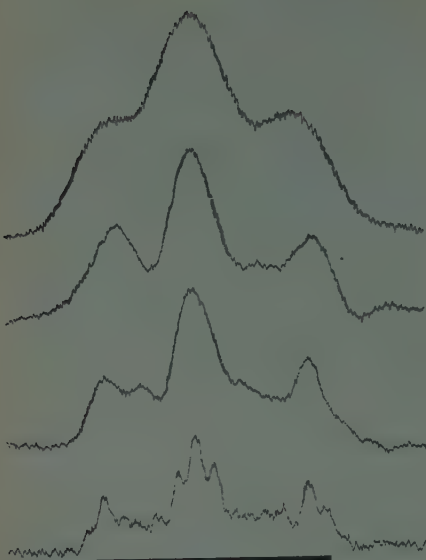


Fig. 3.

Barber's Fig. 2—as a transformation from Fig. 2(b) to 2(d)—keeping in mind, however, that the array length corresponding to the asterisks is fixed at 150 feet. Appropriate switches have been provided in the feeder system so that the various combinations of the array and each of the four interferometer elements may be used. The various antenna beams scan the solar disk in North-South strips and the complete system of array and four elements has recently been tested. Four drift curves for June 28, 1958, are shown in Fig. 3; these were obtained with the array alone, with the array and one interferometer element, with the array and two elements, and with the array and four elements. The approximate East-West beamwidths are, respectively: 8, 4, 2, and 1 minutes of arc. With these increases in resolution, the separation of the three radio emissive sunspot regions from the solar background becomes successively more prominent. The extent of the visible disk, $31'32''$, is shown as a line.

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Potential Well Theory of Velocity Modulation*

The behavior of an electron beam in transit through an accelerating aperture of such velocity modulation devices as klystrons has been described by a bunching theory. It is the purpose of this communication to present another way of viewing the interaction which is based upon a potential well model.

* Received by the IRE, May 8, 1958.

* Received by the IRE, April 28, 1958.
1 B. J. Duncan, L. Swern, and K. Tomiyasu, "Microwave magnetic field in dielectric-loaded coaxial lines," *Proc. IRE*, vol. 46, pp. 500-502; February, 1958.

homogeneous dielectric. Therefore, only the $n=0$ case is of interest for TE modes. Applying the boundary conditions for the $n=0$ case results in the following conditional equations for the even and odd TE modes respectively:

$$k_{x_{2e}} = -k_{x_{1e}} \tanh k_{x_{1e}} a, \quad (5)$$

$$k_{x_{2o}} = -k_{x_{1o}} \coth k_{x_{1o}} a. \quad (6)$$

The subscripts e and o refer to the even and odd modes. In order to have physically realizable propagation in the z direction, it can be shown that $k_{x_{2e}}$ and $k_{x_{2o}}$ must be positive real numbers. Eqs. (5) and (6) show, therefore, that $k_{x_{1e}}$ and $k_{x_{1o}}$ must be pure imaginary numbers and that $(k_{x_{1e}}a)$ and $(k_{x_{1o}}a)$ must be restricted to certain intervals. If we let $k_{x_{1e}} = jk_{x_{de}}$ and $k_{x_{1o}} = jk_{x_{do}}$, where the subscript d refers to the dielectric or region 1, the conditional equations are changed to

$$k_{x_{2e}} = k_{x_{de}} \tan k_{x_{de}} a, \quad (7)$$

$$k_{x_{2o}} = -k_{x_{do}} \cot k_{x_{do}} a. \quad (8)$$

Since the propagation constant (β) must be the same in all regions, the following equations must also be satisfied:

$$k_{x_{de}}^2 - \omega^2 \mu \epsilon_1 = -k_{x_{2e}}^2 - \omega^2 \mu \epsilon_2, \quad (9)$$

$$k_{x_{do}}^2 - \omega^2 \mu \epsilon_1 = -k_{x_{2o}}^2 - \omega^2 \mu \epsilon_2. \quad (10)$$

Substituting (7) into (9) (eliminating $k_{x_{2e}}$), and substituting (8) into (10) (eliminating $k_{x_{2o}}$), we have

$$\pi^2 \left(\frac{2a}{\lambda_0} \right)^2 (K_1 - K_2) = \left[\frac{k_{x_{de}} a}{\cos k_{x_{de}} a} \right]^2 \quad (11)$$

$$\pi^2 \left(\frac{2a}{\lambda_0} \right)^2 (K_1 - K_2) = \left[\frac{k_{x_{do}} a}{\sin k_{x_{do}} a} \right]^2 \quad (12)$$

where $K_1 = \epsilon_1/\epsilon_0$ and $K_2 = \epsilon_2/\epsilon_0$.

Graphical techniques can be used to obtain the distribution constants $k_{x_{de}}$ and $k_{x_{do}}$ after $(2a/\lambda_0)$ and $(K_1 - K_2)$ have been specified.

The final field equations for the symmetric TE modes are given below.

Region 1

$$H_{x1} = A_{1e} \frac{\beta}{k_{x_{1e}}} \cos(k_{x_{de}} x) e^{-\beta z} \quad (13)$$

$$H_{y1} = jA_{1e} \sin(k_{x_{de}} x) e^{-\beta z} \quad (14)$$

$$E_{y1} = A_{1e} \frac{\omega \mu}{k_{x_{de}}} \cos(k_{x_{de}} x) e^{-\beta z} \quad (15)$$

Region 2

$$H_{x2} = A_{1e} \frac{\beta}{k_{x_{2e}}} \sin(k_{x_{de}} a) e^{k_{x_{2e}}(a+x)} e^{-\beta z} \quad (16)$$

$$H_{y2} = -jA_{1e} \sin(k_{x_{de}} a) e^{k_{x_{2e}}(a+x)} e^{-\beta z} \quad (17)$$

$$E_{y2} = -A_{1e} \frac{\omega \mu}{k_{x_{2e}}} \sin(k_{x_{de}} a) e^{k_{x_{2e}}(a+x)} e^{-\beta z} \quad (18)$$

Region 3

The field quantities in Region 3 are the same as in Region 2 except that $e^{k_{x_{2e}}(a+x)}$ is replaced by $e^{k_{x_{2e}}(a-x)}$. The antisymmetric modes are the same as the above except that the roles of the sines and cosines are reversed. The fact that $n=0$ means that there is no variation of the fields in the y direction; that is also shown in (13) through (18).

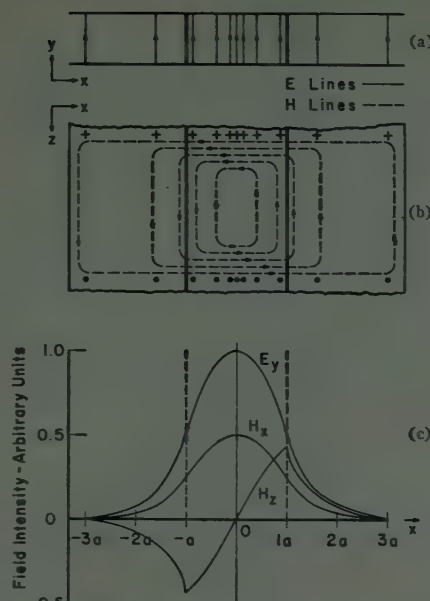


Fig. 2—Field configuration for the dominant mode in parallel plane waveguide partially filled with a dielectric; (a) cross-sectional view, (b) top view, (c) graph of field intensities in a transverse plane.

The mode which is most similar to that shown in Duncan *et al.*¹ is the lowest order even mode (dominant mode) in which

$$0 \leq (k_{x_{de}} a) \leq \frac{\pi}{2}.$$

The field configuration as well as a graph of the field magnitudes are shown in Fig. 2. The magnetic lines are closed loops lying in planes of $y = \text{constant}$ as in Duncan *et al.* The E lines, however, do not have kinks but rather are parallel to the y axis in all three regions. The field distributions in the x direction are sinusoidal or cosinusoidal in the dielectric region, and decay exponentially in the air region. The discrepancy between the two analyses is due to the previously made first-order approximation¹ that the potential difference between the top and bottom plates is a constant in the region of the dielectric.

A similar analysis has been made on TM waves in this structure and, contrary to the previous correspondence,¹ it was found that TM waves could not propagate therein. The propagation of hybrid modes on this type of line has been analyzed by Tischer.^{2,3} It has recently come to the writer's attention that this structure has also been analyzed by Moore and Beam.⁴ This complete paper, however, has not been referenced by the principal indexes in the field. This work appears to have some errors in the equations concerning metallic and dielectric losses.

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¹ F. J. Tischer, "Microwellenleitung mit geringen verlusten." (Waveguides with small losses), *Arch. Elekt. Übertr.*, vol. 7, pp. 592-596; December, 1953.

² F. J. Tischer, "The H -guide, a waveguide for microwaves," 1956 IRE CONVENTION RECORD, pt. 5, pp. 44-47.

³ R. A. Moore and R. E. Beam, "A duo-dielectric parallel plane waveguide," *Proc. NEC*, vol. 12, pp. 689-705; April, 1957.

An Effect of Pulse Type Radiation on Transistors Packaged in a Moist Atmosphere*

In a recent series of experiments on the effects of high-dose rate radiation on transistors, using the Godiva¹ critical assembly of the Los Alamos Scientific Laboratory, an interesting phenomenon was observed.

The investigation of interest consisted of monitoring the transistor collector-to-base leakage current (I_{co}) along a 3-volt, 75-ohm load line, while simultaneously subjecting the transistor to a pulse of neutron plus gamma-ray radiation.

During the pulse of radiation, transistors received a total neutron dose in the order 10^{12} n/cm^2 , and a total gamma dose 10^8 rad in a period of 200 μsec , at rates which varied with time up to a maximum of $10^{17} \text{ n/cm}^2\text{-sec}$ and 10^7 rad/sec for the neutrons and gamma rays, respectively.

Transistors of several types, including $n-p-n$ and $p-n-p$ units of both germanium and silicon were tested in this manner. In all cases the I_{co} vs time characteristic of the form shown in curve A of Fig. 1 was obtained. With one germanium $p-n-p$ type, however, an additional peak was observed as in curve B of Fig. 1. This peak occurred at a much later time and was one to two orders of magnitude smaller than the initial I_{co} transient.

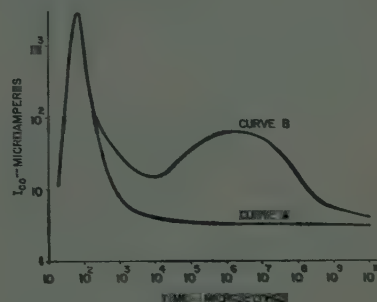


Fig. 1— I_{co} vs time.

All units of this transistor type demonstrated this characteristic behavior (curve B) under test.

Examination of the variations in transistor type, packaging, etc., between this type and all others lead us to believe that the second peak is caused by the presence of water vapor in the transistor case.

This conclusion is based on: 1) the only transistor type to show a second peak was the only transistor packaged in a moist atmosphere and 2) the second peak was not observed in a transistor which differed from the "second peak" type only in that a desiccant was added inside the case.

Work on this phenomenon is continuing in order to arrive at a completely satisfactory mechanism to explain this effect. A possible explanation may be that a partial dehydration of the transistor surface due to

* Received by the IRE, May 19, 1958. This work was performed under AF Contract No. 33 (600) 31315.

¹ R. E. Peterson and G. A. Newby, "An unreflected U-235 critical assembly," *Nuclear Sci. Eng.*, vol. 1, pp. 112-125; May 1956.

radiolysis takes place with a subsequent diffusion outward of the radiolysis products. This is followed by a rehydration of the surface by diffusion of water into the semiconductor. The initial increasing portion of the second peak seems to fit a film diffusion controlled mechanism while the decreasing portion appears compatible with slow first or pseudo-first order kinetics.

We wish to express our thanks to C. H. Zierdt of the General Electric Company for providing us with several specially prepared transistors.

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Theory of the *P-N* Junction Device Using Avalanche Multiplication*

Several devices have been developed which utilize the avalanche multiplication in a reverse-biased junction,¹⁻³ since the nature of the phenomenon was clarified by McKay, *et al.*^{4,5} Among them the three-terminal *p-n-p-n* switch is most versatile in its application.

Avalanche multiplication has been usually understood, after McKay, as the phenomenon that the electron or hole current is multiplied by a constant factor upon passing through a reverse-biased junction. This note points out that this is the case only when the current is composed purely of the electron or hole current on either side of the junction, and proposes a more general, but simple formulation of the phenomenon. This point is important in the central junction of the *p-n-p-n* switch.

According to the atomic theory of the avalanche multiplication,^{6,7} the number of electron-hole pairs created per unit time by an electron or a hole is a complicated function of the electric field acting on it and usually expressed as $\alpha_{en}E$ or $\beta_{hp}E$, where α and β are the ionization rates of electron and hole, respectively, the μ 's represent mobilities, and E , the field strength. The continuity equation for electrons reads

$$-\frac{1}{q} \frac{dI_n}{dx} = \alpha_{en}En + \beta_{hp}Ep, \quad (1)$$

where recombination of carriers is neglected. If we can consider that the current in the space-charge region is mainly composed of drift component⁸ and $\alpha \approx \beta$, (1) becomes

$$(dI_n/dx) = \alpha I, \quad (2)$$

where I is the total current through the junction and is constant. By integration the increment ΔI_n in the electron current upon passing through the junction is shown

$$\Delta I_n = I \int_{\text{depletion layer}} \alpha dx \equiv IA. \quad (3a)$$

Similarly for the hole current

$$\Delta I_p = IA. \quad (3b)$$

Thus, the increments are proportional to total current. If, on either side of the junction, the electron or hole component is nearly equal to the total current

$$\Delta I = I_f - I_i = IA = I_f A,$$

or

$$1 - (1/M) = A = (V/V_B)^n,$$

where V is the applied voltage and V_B the breakdown voltage of the junction. Hitherto this form has been used in the literature. This equation is convenient indeed when applied to the collector junction in an avalanche transistor where the current on the collector side of the collector junction is mainly composed of the carrier of minority to the base region. But when we consider both electron and hole components, it is apt to lead to an incorrect result because of the ambiguous nature of the old formulation.

For example, in the *p-n-p-n* switch in Fig. 1(a), it is shown in the literature³ that the total current at J_2 is

$$I = IM_p\alpha_{1N} + IM_n\alpha_{2N} + I_{CO}. \quad (4)$$

At first sight this seems incorrect. If we evaluate the right side of (4) on the N_B side of J_2 , we must drop M_p in the first term because the hole current emitted at J_1 is not yet multiplied before passing through J_2 , or if we evaluate on the P_B side of J_2 , M_n in the second term must be dropped for the same reason. Fig. 1(b) shows the change of the composition of current according to location in the device.

In our scheme the situation becomes clearer. Consider the N_B side of J_2 . The hole current, which is collected there, is $\alpha_{1N}I$ and the electron current, which is collected and multiplied, is $\alpha_{2N}I + IA$ according to (3a). Therefore the total current is

$$I = I\alpha_{1N} + I\alpha_{2N} + IA + I_{CO}. \quad (5)$$

It is easily shown that the same expression is obtained if we consider the P_B side of J_2 . The condition for breakover is now

$$1 - \alpha_{1N} - \alpha_{2N} = A. \quad (6)$$

This leads to the same expression for breakover voltage V_0 as is obtained from (4):

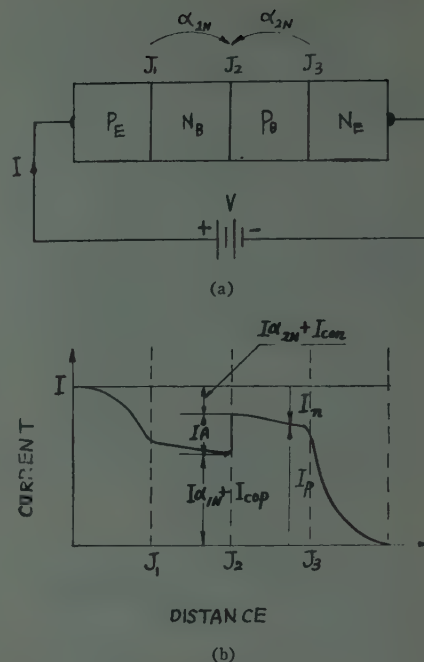


Fig. 1—(a) The structure of *p-n-p-n* switch, (b) composition of current when a small multiplication occurs in the center junction.

$$V_0/V_B = (1 - \alpha_{1N} - \alpha_{2N})^{1/n}.$$

Thus the new formulation is suitable to the case where both electron and hole components are important. It, of course, reduces to the old one if the current on either side of the junction is composed only of electron or hole current.

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Number of Trees in a Graph*

An important property of a linear graph is its number of distinct trees. Trent¹ and Lantieri,² among other authors, have shown how to calculate this number by use of a symmetrical determinant T , and Weinberg³ has used this determinant in applying Kirchhoff's topological laws. If we let n_t represent the total number of nodes of a graph and define $n \equiv n_t - 1$, then n is the order of the determinant T and its elements are given by

t_{ii} = number of branches connected to node i

t_{ik} = -(number of branches connected between nodes i and k) ($i \neq k$).

* Received by the IRE, May 12, 1958.

¹ H. M. Trent, "A note on the enumeration and listing of all possible trees in a connected linear graph," *Proc. Natl. Acad. Sci.*, vol. 40, pp. 1004-1007; October, 1954.

² J. Lantieri, "Méthode de Détermination des Arbres d'un Réseau," *Ann. Télécommun.*, vol. 5, pp. 204-208; May, 1950.

³ L. Weinberg, "Kirchhoff's 'third and fourth laws,'" *IRE TRANS. ON CIRCUIT THEORY*, vol. CT-5, pp. 8-30 March, 1958.

* Received by the IRE, May 15, 1958.

¹ M. C. Kidd, W. Hasenberger, and W. M. Webster, "Delayed collector conduction, a new effect in junction transistors," *RCA Rev.*, vol. 16, pp. 16-33; March, 1955.

² S. L. Miller and J. J. Ebers, "Alloyed junction avalanche transistors," *Bell Sys. Tech. J.*, vol. 34, pp. 883-902; September, 1955.

³ J. L. Moll, M. Tanenbaum, J. M. Goldey, and N. Holonyak, "P-N-P-N transistor switches," *Proc. IRE*, vol. 44, pp. 1174-1182; September, 1956.

⁴ K. G. McKay, "Avalanche breakdown in silicon," *Phys. Rev.*, vol. 94, pp. 877-884; May 15, 1954.

⁵ S. L. Miller, "Avalanche breakdown in germanium," *Phys. Rev.*, vol. 99, pp. 1234-1241; August 15, 1955, and "Ionization rates for holes and electrons in silicon," *Phys. Rev.*, vol. 105, pp. 1246-1249; February 15, 1957.

⁶ P. A. Wolff, "Theory of electron multiplication in Si and Ge," *Phys. Rev.*, vol. 95, pp. 1415-1420; September 15, 1954.

⁷ J. Yamashita, "Theory of electron multiplication in silicon," *Prog. Theor. Phys.*, vol. 15, pp. 95-110; February, 1956.

⁸ This problem was discussed by the writer at the 1956 Annual Meeting of the Physical Society of Japan, July 17, 1956. See also, F. W. G. Rose, "On the impact ionization in the space-charge region of *p-n* junctions," *J. Electronics*, vol. 3, pp. 396-400; October, 1957.

It is thus clear that the elements of the determinant may be found by inspection of the graph. The only problem that remains is the evaluation of the determinant.

When the number of nodes is large, it would appear that evaluation of the determinant is cumbersome. A simple method for evaluating the determinant would therefore be useful. It is the purpose of this note to point out that straightforward evaluation of the determinant is probably never necessary. To illustrate this we show that a formula for the determinant of a complete polygon (or complete graph) is readily found, and then show that formulas for two other special graphs may also be derived.

We define a complete polygon in the usual way as one in which each node is connected to every other node by exactly one branch; examples for $n=3$ and $n=4$ are shown in Fig. 1(a) and 1(b), respectively, where the nodes have been numbered in a clockwise order. It is evident that n branches are connected to each node.

One of the special types of graphs we consider is derived from a complete graph by removing p branches from a single node; thus it is required that $p \leq n$. Without loss of generality the p branches are removed from node 1 and one branch from each of the other nodes $2, 3, \dots, p+1$. An example is shown in Fig. 2 for $n=5$ and $p=2$; the missing branches are shown dashed. The other type of graph is derived from a complete graph by removing a branch from different pairs of nodes, with r being equal to the number of different pairs of nodes with missing branches. Since we permit only one branch to be missing from a node, it is clear that $n \geq 2r$. The graph for which $n=5$ and $r=3$ is given in Fig. 3, where again the missing branches are shown dashed.

For the complete polygon it is found that

$$T = (n+1)^{n-1}. \quad (1)$$

Thus for the graphs in Fig. 1(a) and 1(b) there are 16 and 1296 trees, respectively. For $n=3$ the determinant is

$$T = \begin{vmatrix} 3 & -1 & -1 \\ -1 & 3 & -1 \\ -1 & -1 & 3 \end{vmatrix} \quad (2)$$

and in general the determinant is given by

$$T = \begin{vmatrix} n-1 & -1 & -1 & \dots & -1 \\ -1 & n-1 & -1 & \dots & -1 \\ \dots & \dots & \dots & \dots & \dots \\ -1 & -1 & -1 & \dots & n \end{vmatrix}. \quad (3)$$

Such a special form of determinant is evaluated simply by writing it as the determinant of the sum of a matrix, each of whose elements is -1 , and a diagonal matrix, each of whose elements is $n+1$, and then expanding this determinant about the elements of the diagonal matrix.⁴ However, it is useful in deriving formulas for the other two special types of graphs to make use of the properties of this determinant in another form of evaluation.

Inspection of (2) shows that the sum of the elements in each column is equal to

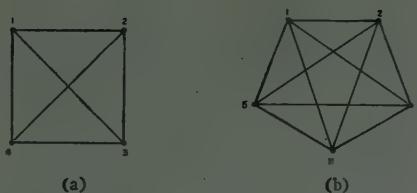


Fig. 1—Complete polygons for $n=3$ and $n=4$.

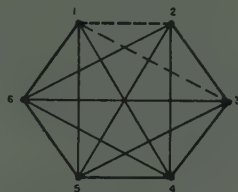


Fig. 2—Graph for $n=5$ and $p=2$.

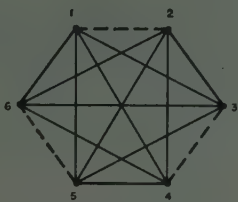


Fig. 3—Graph for $n=5$ and $r=3$.

unity. This property, it is clear, is true for all n . Therefore, if all of the succeeding rows are added to the first, the latter becomes a row of ones, and

$$T = \begin{vmatrix} 1 & 1 & 1 \\ -1 & 3 & -1 \\ -1 & -1 & 3 \end{vmatrix}. \quad (4)$$

Then the first row is added successively to each of the other rows to give

$$T = \begin{vmatrix} 1 & 1 & 1 \\ 0 & 4 & 0 \\ 0 & 0 & 4 \end{vmatrix} \quad (5)$$

whose value is now obtained by inspection. By the same reasoning we can show that in general $T = (n+1)^{n-1}$.

Making use of these properties allows the other formulas to be derived. For example, for the graph in Fig. 3 we have

$$T = \begin{vmatrix} 4 & 0 & -1 & -1 & -1 \\ 0 & 4 & -1 & -1 & -1 \\ -1 & -1 & 4 & 0 & -1 \\ -1 & -1 & 0 & 4 & -1 \\ -1 & -1 & -1 & -1 & 4 \end{vmatrix} \quad (6)$$

which is transformed to

$$T = \begin{vmatrix} 1 & 1 & 1 & 1 & 0 \\ 0 & 4 & -1 & -1 & -1 \\ 0 & 0 & 5 & 1 & -1 \\ 0 & 0 & 1 & 5 & -1 \\ 0 & 0 & 0 & 0 & 4 \end{vmatrix}. \quad (7)$$

To obtain (7) from (6) we added all the succeeding rows to the first row, and then added the new first row successively to the 3rd, 4th, and 5th rows. The determinant is now readily evaluated as

$$\begin{aligned} T &= 4 \begin{vmatrix} 5 & 1 & -1 \\ 1 & 5 & -1 \\ 0 & 0 & 4 \end{vmatrix} \\ &= 4^2(5^2 - 1) \\ &= 4^2(61) \\ &= 384. \end{aligned} \quad (8)$$

By performing the same types of operations on the T for a graph in which $n=7$ and $r=4$, we find

$$\begin{aligned} T &= 6^4 8^2 \\ &= 16,384. \end{aligned} \quad (9)$$

The answers are given in the form of the next to the last equation of (8) and (9) because this form suggests the general formula. In fact, we find that the number of trees in a graph in which there are r pairs of nodes with missing branches is given by

$$T = (n-1)^r(n+1)^{n-1-r}. \quad (10)$$

Here $n \geq 1$ and $n+1 \geq 2r$.

Similarly, for a graph in which there are p branches missing from one node we derive that the number of trees is

$$T = n^{p-1}(n-p)(n+1)^{n-1-p}. \quad (11)$$

Here $n \geq 1$ and $p \leq n$.

We thus conclude that because of the special form of the determinant its evaluation is not computationally difficult. To eliminate the necessity of evaluating the determinant for three special types of graphs, formulas have been derived for these cases.

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Algebraic Approach to Signal Flow Graphs*

Much has been written about networks consisting of unilateral elements exclusively, i.e., signal flow graphs, in particular by Mason^{1,2} who has provided us with a complete set of topological rules for the analysis of such networks (and of others³). The usefulness of these rules cannot be doubted, but everyone cannot spend the time required for their mastery especially when the usual tools of matrix analysis are readily available. Therefore, this note indicates an orderly, i.e., matrix, method of analyzing signal flow graphs. Incidentally, this approach could serve as a convenient starting point for the proof of some of the topological rules.

Let $T_{\alpha\beta}$ denote the transmittance pointing from node α to node β , and put $T_{\alpha\alpha} = 1$ for all input nodes; let v_α be the node to

* Received by the IRE, May 19, 1958.

¹ S. J. Mason, "Feedback theory—some properties of signal flow graphs," *Proc. IRE*, vol. 41, pp. 1144–1156; September, 1953.

² S. J. Mason, "Feedback theory—further properties of signal flow graphs," *Proc. IRE*, vol. 44, pp. 920–926; July, 1956.

³ S. J. Mason, "Topological analysis of linear non-reciprocal networks," *Proc. IRE*, vol. 45, pp. 829–838; June, 1957.

⁴ A. C. Aitken, "Determinants and Matrices," Oliver and Boyd Ltd., Edinburgh and London, p. 87 and ex. 2, p. 133; 1956.

datum voltage of node α , then

$$v_\beta = \sum_{\alpha} T_{\alpha\beta} v_\alpha \quad (1)$$

Forming voltages into vector v and transmittances into the square matrix T , we write for (1)

$$v = T v, \quad (2)$$

T_t being the transpose of T . Equivalently, denoting by I the unit matrix,

$$(T_t - I)v = 0. \quad (3)$$

This equation solves the network. Note that v contains the inputs as well as the driven voltages.

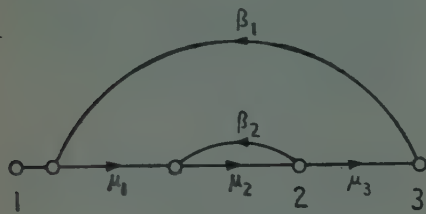


Fig. 1.

As a specific example consider Fig. 1, where the hollow circles denote mixing points. In order to analyze this situation without the use of additional rules, a sufficient number of nodes to break all loops must be identified. In our example one node is required in addition to the input terminal. By inspection,

$$T - I = \begin{bmatrix} 0 & \mu_1 \mu_2 \\ 0 & \beta_2 \mu_2 + \mu_3 \beta_1 \mu_2 - 1 \end{bmatrix}.$$

Denoting cofactors by superscripts we find for the through transmittance H_{13} ,

$$\begin{aligned} -\mu_3 H_{13} &= \mu_3 \frac{V_2}{\Gamma_1} = \mu_3 \frac{(T_t - I)^{12}}{(T_t - I)^{11}} \\ &= \mu_3 \frac{(T - I)^{21}}{(T - I)^{11}} \\ &= \frac{\mu_1 \mu_2 \mu_3}{1 - \mu_2 \beta_2 - \mu_1 \mu_2 \mu_3 \beta_1}. \end{aligned}$$

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On the Coupling Coefficients in the "Coupled-Mode" Theory*

The "coupled-mode" theory has proved itself to be an important tool in the analysis of energy exchange phenomena between traveling waves. In its original form¹ it is capable of yielding important qualitative results. To extend its range of usefulness into the quantitative domain, one needs to evaluate the coupling coefficients which govern

the energy exchange. This is done in this paper where we treat the "small coupling" case. We assume that in obtaining the coupling coefficients for the small coupling case we may use for the different physical observables their values in the absence of coupling. This procedure is analogous to that used in evaluating the Q of a cavity or the attenuation constant of a waveguide, for the small loss case, where the loss-free field solutions are used instead of the actual solutions in the presence of losses, and is a type of perturbation theory formulated on physical grounds.

Using Haus's² formulation of Pierce's coupled-mode theory we write for the system of differential equations obeyed by the mode amplitudes

$$\frac{d[A]}{dz} = [C][A], \quad (1)$$

$[A]$ is a column matrix, whose individual components $A_i(z)$ are normalized such that $\pm A_i A_i^*$ is the power carried by the i th mode in the $+z$ direction, the z direction being taken as the direction of propagation. $[C]$ is a square matrix whose determination is the subject of this paper.

The condition of power conservation yields:

$$C_{ki}^* = \mp C_{ik} \quad k \neq i \quad (2)$$

where the upper and lower signs apply when modes i and k carry power in the same or opposite directions, respectively. Using (1) and (2) we get:

$$C_{mn} = \frac{\frac{d}{dz}(A_m A_n^*)}{2 \operatorname{Re}(A_m^* A_n)} \quad (3)$$

for C_{mn} real.

$$C_{mn} = j \frac{\frac{d}{dz}(A_m A_n^*)}{\operatorname{Im}(A_m A_n^*)} \quad (4)$$

for C_{mn} imaginary.

A_m and A_n have to be defined in terms of the physical observables (fields, current, etc.) in such a way that either $\operatorname{Re}(A_m A_n^*)$ is proportional to the distance rate of change of power in mode m (or n), in which case (3) applies or $\operatorname{Im}(A_m A_n^*)$ is proportional to the power rate of change, in which case (4) applies. The proportionality constant is real in both cases.

To illustrate the application of the theory we treat the cases of the traveling-wave tube and the double stream amplifier.

TRAVELING-WAVE TUBE

The coupled-modes are the "fast" and "slow" space-charge waves and the circuit-forward wave (the circuit-backward wave is assumed matched out).

Let:

$$A_n A_n^* = \frac{V V^*}{2K} = \frac{E_s E_s^*}{2\beta_c^2 K} \quad (5)$$

where

K = field-normalized circuit impedance,³
 E_s = effective axial field,

* H. Haus, "Coupled Mode Theory," M.I.T., Cambridge, Mass., unpublished report.

¹ J. R. Pierce, "Traveling-Wave Tubes," D. Van Nostrand Co., Inc., New York, N. Y., 1950.

β_c = free (uncoupled) propagation constant of the circuit. In its free state the beam carries RF kinetic power P_K

$$P_K = -\frac{A u_0}{2\eta} \operatorname{Re}(v_s i_s^*) \quad (6)$$

where

A = beam cross-section area,
 u_0 = beam dc velocity,
 $\eta = |e/m|$ = charge to mass ratio of the electron,
 v_s, i_s are the beam ac velocity and current density, respectively.

For a single space-charge wave (6) can be rewritten as:

$$P_K = A_m A_m^* = \frac{\omega_0 V_0}{\omega I_0} I_s I_s^* \quad (7)$$

where:

ω_0, ω = beam reduced plasma frequency and frequency, respectively,
 V_0, I_0 = beam dc voltage and current, respectively,
 I_s = beam ac current.

In view of (6) and (7) we can write

$$A_m = \left(\frac{\omega_0 V_0}{\omega I_0} \right)^{1/2} I_s \quad (8)$$

$$A_n = \frac{1}{(2K)^{1/2} \beta_c} E_s. \quad (9)$$

Employing Poynting's theorem we can show that the rate of change of circuit power is given by:

$$\frac{d}{dz}(A_n A_n^*) = -\frac{1}{2} \operatorname{Re}(E_s I_s^*)$$

using (8)–(10) and assuming

$$\beta_c \approx \frac{\omega}{u_0} = \beta_s, \quad (10)$$

we get:

$$C_{mn}^2 = S^2 = \frac{\beta_s^3 C^3}{2\beta_q} \quad (11)$$

S being defined by (11).

Taking A_1 as the forward-circuit mode, A_2 and A_3 as the "fast" and "slow" space-charge wave, and assuming $C_{23} = 0$ and $e^{-\Gamma z}$ propagation, (1) becomes

$$\begin{aligned} (-j\beta_c + \Gamma)A_1 + SA_2 + SA_3 &= 0 \\ -SA_1 + [-j(\beta_s - \beta_q) + \Gamma]A_2 &= 0 \\ SA_1 + [-j(\beta_s + \beta_q) + \Gamma]A_3 &= 0 \end{aligned} \quad (12)$$

resulting in the determinantal equation:

$$j\beta_s^2 \beta_c - \beta_s^2 \Gamma - j\beta_q^2 \beta_c + \beta_q^2 \Gamma - 2\beta_s \beta_c \Gamma - j\beta_c \Gamma^2 - 2j\beta_s \Gamma^2 + \Gamma^3 - 2j\beta_s S^2 = 0. \quad (13)$$

Eq. (13) can be solved directly for Γ . To cast the result in a more familiar form we adopt the convention:

$$\begin{aligned} -\Gamma &= -j\beta_s + \beta_s c\delta \\ \beta_c &= \beta_s(1 + cb) \\ \beta_q &= \beta_s(4QC^2)^{1/2}. \end{aligned}$$

Eq. (13) becomes the well-known equation for the traveling-wave tube³

$$(\delta^2 + 4QC)(-b + j\delta) = +1. \quad (14)$$

* Received by the IRE, May 26, 1958.

¹ J. R. Pierce, "Coupling of modes of propagation," *J. Appl. Phys.*, vol. 25, pp. 179–183; February, 1954.

It should be noted that in no place have we used results from other traveling-wave tube theories. We have merely adopted some of Pierce's conventional symbols in order to arrive at (14).

DOUBLE STREAM AMPLIFIER

The interaction is assumed to take place between the "slow" space-charge wave of the fast electron beam, called A_2 , and the "fast" space-charge wave of the slow beam, denoted as A_1 . The slow and fast electron beams have equal charge densities and have dc velocities u_{01} and u_{02} , respectively.

Using results of the kinetic power theorem in a way analogous to that leading to (8) we get:

$$A_1 = \left(\frac{u_{01}\omega_q}{2\eta\omega | \rho_0 | A} \right)^{1/2} I_1, \quad (15)$$

$$A_2 = \left(\frac{u_{02}\omega_q}{2\eta\omega | \rho_0 | A} \right)^{1/2} I_2. \quad (16)$$

In analogy with (10) we get:

$$\frac{d}{dz} (A_1 A_1^*) = -\text{Re} (E_1 I_2^*). \quad (17)$$

Using (15)–(17) in (4) plus the result:

$$E_1 = \frac{jI_1}{\omega \epsilon A}$$

leads to

$$C_{12} = -j \frac{\omega_p^2}{\omega_q (u_{01} u_{02})^{1/2}} \quad (18)$$

and a determinantal equation whose solution, assuming $e^{-j\beta z}$ propagation, is:

$$\beta_{1,2} = \frac{\beta_{01} + \beta_{02}}{2} \pm \left[\left(\frac{\beta_{01} - \beta_{02}}{\sqrt{2}} \right)^2 - |c_{12}|^2 \right]^{1/2} \quad (19)$$

where:

$$\beta_{01} = \frac{\omega}{u_{01}} - \frac{\omega_q}{u_0} = \frac{\omega}{u_{01}} - \beta_q$$

$$\beta_{02} = \frac{\omega}{u_{02}} + \frac{\omega_q}{u_0} = \frac{\omega}{u_{02}} + \beta_q.$$

Defining:

$$u_{01} = u_0(1 - b)$$

$$u_{02} = u_0(1 + b)$$

$$\beta_{1,2} = \beta_0(1 \pm \delta_{1,2}), \quad x = \frac{b\beta_q}{\beta_0}$$

and assuming

$$b^2 \ll 1, \quad \frac{\beta_p}{\beta_0} < 1, \quad \beta_p = \beta_q$$

leads to:

$$\delta_{1,2} = \pm \frac{\beta_p}{\beta_0} [(1+x^2) - (1+4x^2+4x)^{1/2}]^{1/2}. \quad (20)$$

The "classical" small signal analysis yields:⁴

$$\delta_{1,2} = \pm \frac{\beta_p}{\beta_0} [(1+x^2) - (1+4x^2)^{1/2}]^{1/2}. \quad (21)$$

⁴ A. B. Haef, "The electron-wave tube—a novel method of generation and amplification of microwave energy," *Proc. IRE*, vol. 37, pp. 4–10; January, 1949.

The difference between the two results is believed to be due to the failure of our two-mode picture to take into account the two extreme modes. Some of the differences are shown in Table I.

TABLE I

Feature	Small Signal (Haef)	Coupled Modes (Two-Modes Approximation)
Maximum Gain at Maximum Gain of Gain Obtained for	$x = \frac{1}{2}\sqrt{3}$ $\frac{1}{2}(\omega_p/\omega)$ nepers $0 < x < \sqrt{2}$	$x = 1.0$ ω_p/ω nepers $0 < x < 2$

We are aware of the fact that this problem has been recently solved in a more formal manner by Haus of M.I.T. We believe that the approximate perturbation solution given here may still prove useful.

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Effect of Beam Coupling Coefficient on Broad-Band Operation of Multicavity Klystrons*

To meet some of the requirements of present-day electronic systems, attention has recently been focused on the problem of broad-band operation of multicavity klystrons.^{1–7} The major advantages of using broad-band multicavity klystrons at high-power levels (in comparison with a TWT operating over the same bandwidth) presumably are 1) no backward wave is present (as the multicavity-klystron structure is not bilateral) and the attenuator problem (which is present in a TWT) may be eliminated, and 2) possible better efficiency in the case of a multicavity klystron than in a TWT. This statement is based on the fact that under

* Received by the IRE, May 19, 1958.
¹ K. H. Kreuchen, B. A. Auld, and N. E. Dixon, "A study of the broadband frequency response of the multicavity klystron amplifier," *J. Electron-ics*, vol. 2, p. 529; May, 1957.

² L. D. Smullin and A. Bers, "Stagger Tuned Multicavity Klystron," Conference on Electron Tube Res., Berkeley, Calif.; 1957.

³ S. V. Yadavalli, "Application of the potential analog in multicavity klystron design and operation," *Proc. IRE*, vol. 45, pp. 1286–1287; September, 1957. Also presented in collaboration with C. A. Arnold and J. P. Lindley at the Conference on Electron Tube Res., 1957.

⁴ W. J. Dodds, T. Moreno, and W. J. McBride, Jr., "Methods of increasing bandwidth of high power microwave amplifiers," 1957 WESCON CONVENTION RECORD, pt. 3, pp. 101–110.

⁵ W. L. Beaver, R. L. Jepsen, and R. L. Walter, "Wide band klystron amplifiers," 1957 WESCON CONVENTION RECORD, pt. 3, pp. 111–113.

⁶ P. G. R. King, "A five per cent bandwidth 2.5 mw s-band klystron," *SERL Tech. J.*, vol. 8, p. 29; January, 1958.

⁷ H. T. Curnow, "Factors influencing the design of multicavity klystrons," *SERL Tech. J.*, vol. 8, p. 42; January, 1958.

synchronously tuned conditions, a typical high-power klystron can have an efficiency in the neighborhood of 40 per cent.

In a discussion of broad-band operation of multicavity klystrons, one comes across the question: "Under what conditions is the broad-band operation of multicavity klystrons profitable?"

A suitable starting point for a discussion of the above problem is the relation

$$V^{(0)} = MZ^{(0)}i \quad (1)$$

where M and $Z^{(0)}$ are the beam coupling coefficient and shunt impedance of the output cavity, respectively, and i is the ac current in the beam at the entrance to the output cavity. We note that the maximum voltage across the output gap $V_{\max}^{(0)}$ which we can best use is the dc voltage of the beam V_0 ; this is so because, for any value of $V^{(0)}$ larger than the dc beam voltage V_0 , electrons would be reflected at the output gap and they will travel toward the input. It is also known that i_{\max} (the maximum ac current in the beam at the output gap) is approximately equal to the dc current (for instance under ballistic assumptions $i_{\max} = 1.16I$).

Hence, under the optimum conditions for power transfer from the output cavity, we may write

$$V^{(0)} \approx V_0 \approx MZ^{(0)}I \quad (2)$$

or

$$Z^{(0)} \approx Z_0 \quad (2a)$$

when

$$M \approx 1$$

$$Z_0 = \frac{V_0}{I}$$

Z_0 being the dc beam impedance, and I the dc current of the beam at input.

We may also write

$$Z^{(0)} = (R/Q)_0 Q_L^{(0)} \quad (3)$$

where $(R/Q)_0$ and $Q_L^{(0)}$ are the values of R/Q and Q of the output cavity under loaded conditions. From (3) we note that for optimum performance $Q_L^{(0)}$ is specified when once the beam voltage V_0 and dc beam current I are specified. In practice, however, the relation $Z^{(0)} \approx Z_0$ is not always satisfied. Many klystron engineers choose values of $Q_L^{(0)}$ based on experience which are at variance with the above simple relation. Actually the shunt impedance across the output gap is made several times the value of beam impedance Z_0 at higher frequencies. We note that as $Z^{(0)}$ goes up the value of $Q_L^{(0)}$ goes up or equivalently $Q_E^{(0)}$ goes up ($Q_E^{(0)}$ being the external Q of the output cavity).

Since RF power is extracted from the output cavity, it is clear that the same (the output cavity) determines the bandwidth over which efficient power transfer can be effected.

We will now discuss the problem as follows. The bunched beam as it enters the output gap exhibits a velocity distribution which in turn alters the value of the beam coupling coefficient considerably. The usual value of beam coupling coefficient M for a gridless gap is given by

$$M = \frac{I_0(\gamma_0 r_0)}{I_0(\gamma_0 b_0)} \frac{\sin \omega d g / 2u_0}{\omega d g / 2u_0} \quad (4)$$

where:

I_0 denotes a Bessel function
 γ_0 = the radial propagation constant

$$\left(\gamma_0 = \frac{\omega}{u_0} \sqrt{1 - u_0^2/c^2} \right)$$

u_0 = dc beam velocity corresponding to the dc voltage V_0

ω = the operating frequency, c the velocity of light

d_g = the gap length,

r_0 and b_0 = the radii of the beam and drift tube, respectively.

In calculating the loaded $Q(Q_L^{(0)})$ of the output cavity for optimum performance, we need to use the average value of the beam coupling coefficient. If the velocity distribution of the bunched beam is specified by a probability distribution $P(u)$, assuming the velocity distribution is uniform over the beam cross section, we can write the average beam coupling coefficient as

$$\langle M \rangle_{av} = \frac{1}{N+1} \sum_{n=0}^N \left\{ \int_{u_1}^{u_2} \frac{I_0(\gamma R_n)}{I_0(\gamma b_0)} \frac{\sin \omega d g / 2u}{\omega d g / 2u} \cdot P(u) du \right\} \quad (5)$$

where N is the number of equal parts into where r_0 is divided $R_n = nr_0/N$, n is a dummy index, d_g is the output gap length, u is the beam velocity and

$$\gamma = \frac{\omega}{u} \sqrt{1 - u^2/c^2}.$$

We also have $\int_{u_1}^{u_2} u P(u) du = 1$, where u_1 and u_2 are the lowest and highest velocities of the electrons in the beam. Employing the velocity distributions near saturation obtained by Webber⁸ recently, the above value of $\langle M \rangle_{av}$ has been computed for several cases. One should remember that there are two types of velocity distributions of interest here, 1) as the beam enters and 2) as the beam leaves the output gap. That is, we can calculate two types of average beam coupling coefficients $\langle M \rangle_{av}^i$ and $\langle M \rangle_{av}^o$ where the superscripts i and o denote the corresponding velocity distributions employed whether at input or output of the output gap. Wherever Webber's distributions were not available, estimates have been made regarding the velocity distribution.

As the power output is proportional to $\langle M \rangle_{av}^2$, one is essentially interested in a plot of $\langle M \rangle_{av}^2$ vs $\gamma_0 r_0$. In Fig. 1 it is assumed that the gap transit angle is

$$60^\circ \left(= \frac{\omega d g}{u_0} \right),$$

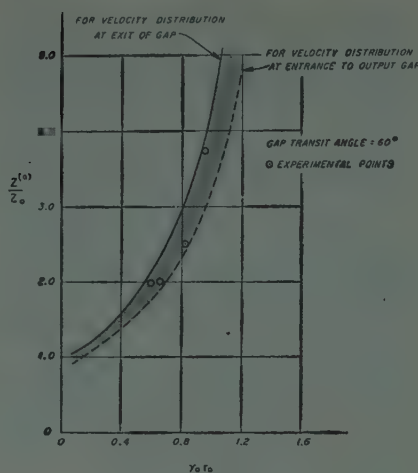


Fig. 1—Plot of normalized output gap impedance vs $\gamma_0 r_0$.

and the RF current in the beam is $1.1I$. Two curves are shown corresponding to the two limiting velocity distributions in Fig. 1; some experimental points observed in this laboratory and elsewhere are also shown here for comparison. We may indicate here that if one uses the velocity distribution at the middle of the gap in the calculation of $\langle M \rangle_{av}$ we should be able to predict the value of shunt impedance (across the output cavity) very close to the actual value which in turn determines $Q_L^{(0)}$ and $Q_E^{(0)}$ when the unloaded Q of the cavity is known.

In practice the beam radii that are chosen in klystrons operating at different frequencies are such that $\gamma_0 r_0$ goes up with frequency. As mentioned before $Z^{(0)} = kZ_0$ where k is usually greater than unity. We conclude then that it is better to build broad-band klystrons with small $\gamma_0 r_0$. To state differently, this means that for a given value of Γ_0 1) it is better to build broad-band multicavity klystrons at lower frequencies (that is, a broad-band multicavity klystron at L band would be more profitable than the one at S band as far as bandwidth and efficiency are concerned) and 2) it is better to operate broadband multicavity klystrons at higher voltages (also higher perveances) than the synchronously tuned klystrons.

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Improvements in Some Bounds on Transient Responses*

Consider a system function $Z(s)$ of a lumped, linear, fixed, finite, and stable network, all of whose poles have negative (non-zero) real parts. Moreover, assuming that the number of poles of $Z(s)$ is equal to or greater than the number of zeros of $Z(s)$, this rational system function may be ex-

panded into the following infinite series, for s is sufficiently large,

$$Z(s) = K + \frac{1}{Cs} + \frac{K_2}{s^2} + \dots$$

In the neighborhood of $s=0$, $Z(s)$ may be represented by

$$Z(s) = r + k_1 s + k_2 s^2 + \dots$$

It has been shown recently that when the real frequency responses ($s=j\omega$) of $Z(s)$ are restricted in various ways, the corresponding transient responses are bounded. The purpose of this note is to report improvements on some of these results. In particular, denoting the real part of the system function at real frequencies by $R(\omega)$ and the corresponding response to a unit impulse of current applied at $t=0$ by $W(t)$, these two functions may be related by the following Fourier cosine transform:

$$W(t) = \frac{2}{\pi} \int_0^\infty R(\omega) \cos \omega t d\omega, \quad t \geq 0.$$

In this case, the specific result which is to be improved is given by theorem 2 of Zemanian¹ wherein bounds on $W(t)$ are given when $R(\omega)$ is monotonic decreasing for $\omega \geq 0$. The improved result is stated by the following theorem. Both the upper and lower bounds are now best possible so that no further improvement can be made.

Theorem: If $Z(s)$ is a system function satisfying the aforementioned restrictions, if the number of poles of $Z(s)$ is one greater than the number of its zeros, and if $R(\omega)$ is monotonic decreasing for $\omega \geq 0$, then the lowest possible upper bound on all unit impulses corresponding to such $Z(s)$ is

$$W(t) \leq \frac{1}{C} \cdot \frac{\sin \frac{\pi t}{2rC}}{\frac{\pi t}{2rC}} \quad \text{for } 0 \leq t \leq rC$$

and

$$W(t) \leq \frac{2r}{\pi t} \quad \text{for } rC \leq t$$

and the greatest possible lower is

$$W(t) \geq \frac{1}{C} \cdot \frac{\sin \frac{\pi t}{\theta_1}}{\frac{\pi t}{\theta_1}} \quad \text{for } 0 < t \leq \frac{2rC\theta_1}{\pi},$$

$$W(t) \geq \frac{1}{C} \cdot \frac{\sin \frac{\pi t}{2rC}}{\frac{\pi t}{2rC}} \quad \text{for } \frac{2rC\theta_1}{\pi} \leq t \leq 3rC.$$

and

$$W(t) \geq -\frac{2r}{\pi t} \quad \text{for } 3rC \leq t$$

where θ_1 is the number satisfying $\theta_1 = \tan \theta_1$ and $\pi < \theta_1 < 3\pi/2$ (that is, $\theta_1 = 4.49 \dots$).

Proof of this theorem has been published elsewhere² and will not be repeated here.

It should be pointed out that this result applies to any two variables that are related by the Fourier cosine transform. For in-

* S. E. Webber, "Ballistic Analysis of a Two-Cavity Ferrite Beam Klystron," G. E. Res. Lab., Palo Alto, Calif., Rep. No. 57-RL-1721; April, 1957.

Also see, "Large Signal Analysis of the Multicavity Klystron," G. E. Res. Lab., Palo Alto, Calif., Memo Rep. No. EE-39; June, 1957.

There is additional unpublished work.

These calculations were carried out on electronic computers IBM 704 and 650.

* Received by the IRE, May 19, 1958.

¹ A. H. Zemanian, "Further bounds existing on the transient responses of various types of networks," Proc. IRE, vol. 43, pp. 322-326; March, 1955.

² A. H. Zemanian, "Bounds on the Fourier transforms of monotonic functions," Duke Math. J., vol. 24, pp. 499-504; December, 1957.

stance, if the symbol $R(\omega)$ represents the power-density function of a random signal, then $W(t)/4$ will represent the corresponding autocorrelation function.

This property of the Fourier cosine transform may be applied to the response $A(t)$ of a network to a unit step of current applied at $t=0$, since $A(t)$ is related to the imaginary part $I(\omega)$ of the system impedance at real frequencies by the following expression.

$$A(t) = r + \frac{2}{\pi} \int_0^\infty \frac{I(\omega)}{\omega} \cos \omega t d\omega, \quad t \geq 0.$$

This leads to the following theorem whose proof is practically the same. The stated bounds are, once again, best possible.

Theorem: If $Z(s)$ is a system function satisfying the aforementioned restrictions and if $I(\omega)/\omega$ is monotonic increasing for $\omega \geq 0$, then the lowest possible upper bound on all unit step responses corresponding to such $Z(s)$ is

$$1(t) \leq r - (r - K) \frac{\sin \theta_1}{\theta_1} \quad \text{for } 0 < t \leq \frac{2\theta_1 k_1}{\pi(r - K)},$$

$$A(t) \leq r - (r - K) \frac{\sin \frac{\pi(r - K)t}{2k_1}}{\frac{\pi(r - K)t}{2k_1}} \quad \text{for } \frac{2\theta_1 k_1}{\pi(r - K)} \leq t \leq \frac{3k_1}{(r - K)},$$

and

$$A(t) \leq r + \frac{2k_1}{\pi t} \quad \text{for } \frac{3k_1}{(r - K)} \leq t$$

and the greatest possible lower bound is

$$A(t) \geq r - (r - K) \frac{\sin \frac{\pi(r - K)t}{2k_1}}{\frac{\pi(r - K)t}{2k_1}} \quad \text{for } 0 < t \leq \frac{k_1}{(r - K)}$$

and

$$A(t) \geq r - \frac{2k_1}{\pi t} \quad \text{for } \frac{k_1}{(r - K)} \leq t$$

where θ_1 is defined in the first theorem.

An immediate consequence of this theorem is that, for system functions of the stated type, the overshoot of the unit step response—defined as the greatest value of $[A(t) - r]/r$ —is never greater than $|\sin \theta_1/\theta_1| = 0.2172$ and the rise time from $t=0$ to the time when the unit step response first equals r has no positive lower bound.

Finally, a similar result is shown to hold on any two variables that are related by the Fourier sine transforms.² However, this result is not readily applicable to the unit impulse response since it assumes that the imaginary part of the system function is monotonic decreasing for positive ω . This is impossible for the networks considered here.

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Geometric-Analytic Theory of Noisy Two-Port Networks*

In two recent notes in this journal^{1,2} an outline on the manner in which the Cayley-Klein model of three-dimensional hyperbolic space can be used in studying problems dealing with bilateral two-port networks was presented. By a stereographic transformation, points in the complex impedance plane were mapped on the surface of the unit sphere constituting the absolute surface of the Cayley-Klein model. Now a natural question is: "What physical interpretation can we give to points inside the surface of the unit sphere?" The answer is that these points may be thought of as corresponding to noise-power ratios. Thus, noise-power ratio transformations through noise-free bilateral two-port networks can be geometrically represented by non-Euclidean transformations in models of three-dimensional hyperbolic space. The special case of impedance transformations through noise-free bilateral two-port networks is obtained as non-Euclidean transformations of points on the absolute surfaces of the different models.

The input voltage V' and the input current I' of a noise-free bilateral two-port network are linearly related to the output voltage V and the output current I :

$$\psi' = \begin{pmatrix} V' \\ I' \end{pmatrix} = \begin{pmatrix} a & b \\ c & d \end{pmatrix} \begin{pmatrix} V \\ I \end{pmatrix} = T\psi, \quad ad - bc = 1. \quad (1)$$

The input impedance $Z' = V'/I'$ is expressed in terms of the output impedance $Z = V/I$ by the linear fractional transformation:

$$Z' = \frac{aZ + b}{cZ + d}. \quad (2)$$

For a noise process, transformed by a noise-free two-port network, (1) and (2) are exchanged for

$$Q' = \begin{pmatrix} Q_1' \\ Q_2' \\ Q_3' \\ Q_4' \end{pmatrix} = \begin{pmatrix} \overline{V'V'^*} \\ \overline{V'I'^*} \\ \overline{V'I'^*} \\ \overline{I'I'^*} \end{pmatrix} = \begin{pmatrix} aa^* & ab^* & ba^* & bb^* \\ ac^* & ad^* & bc^* & bd^* \\ ca^* & cb^* & da^* & db^* \\ cc^* & cd^* & dc^* & dd^* \end{pmatrix} \begin{pmatrix} \overline{VV^*} \\ \overline{VI^*} \\ \overline{V'I^*} \\ \overline{II^*} \end{pmatrix} \quad (3)$$

and

$$s'^2 = \frac{Q_1'}{Q_4'} = \frac{aa^*s^2 + ab^*Z_{\text{cor}} + ba^*Z_{\text{cor}}^* + bb^*}{cc^*s^2 + cd^*Z_{\text{cor}} + dc^*Z_{\text{cor}}^* + dd^*} \quad (4a)$$

$$Z'_{\text{cor}} = \frac{Q_2'}{Q_4'} = \frac{ac^*s^2 + ad^*Z_{\text{cor}} + bc^*Z_{\text{cor}}^* + bd^*}{cc^*s^2 + cd^*Z_{\text{cor}} + dc^*Z_{\text{cor}}^* + dd^*} \quad (4b)$$

$$Z'^*_{\text{cor}} = \frac{Q_3'}{Q_4'} = \frac{ca^*s^2 + cb^*Z_{\text{cor}} + da^*Z_{\text{cor}}^* + db^*}{cc^*s^2 + cd^*Z_{\text{cor}} + dc^*Z_{\text{cor}}^* + dd^*} \quad (4c)$$

Asterisks indicate the complex conjugate of the designated quantities and bars indicate averages over an ensemble of noise processes with identical statistical properties.

* Received by the IRE, May 19, 1958.

¹ E. F. Bolinder, "Noisy and noise-free two-port networks treated by the isometric circle method," Proc. IRE, vol. 45, pp. 1412-1413; October, 1957.

² E. F. Bolinder, "Radio engineering use of the Cayley-Klein model of three-dimensional hyperbolic space," to be published.

In the case of complete correlation, $s'^2 = ZZ^*$, with $Z_{\text{cor}} = Z$, and (4a) reduces to $s'^2 = Z'Z'^*$, with $Z'_{\text{cor}} = Z'$; (4b) reduces to (2), and (4c) reduces to the complex conjugate of (2).

The four-vector Q in (3) is analogous to the "Stokes vector" used by Stokes in 1852 in characterizing partially polarized light. The 4×4 matrix in (3) has been used in optics by Soleillet, Perrin, Chandrasekhar, Mueller, Parke, and others. It is the Kronecker product, $T \times T^*$, of the 2×2 matrix T in (1). The components of the Q vector are the components of a 2×2 Hermitian coherency matrix analogous to the "density matrix" introduced in quantum mechanics by von Neumann, and the "coherency matrix" introduced in optics by Wiener.

The conformal transformation (4) can be considered to be a non-Euclidean transformation in a Poincaré model of three-dimensional hyperbolic space having the Z_{cor} plane as the absolute surface. The transformation has been thoroughly studied by Poincaré,³ Picard,⁴ Fricke and Klein,⁵ and others.

Eqs. (3) and (4) have been used as the basis of a general theory of noisy two-port networks.⁶ Among the topics treated are a wave representation of noisy two-ports (with the introduction of a complex correlation-reflection coefficient), the equivalent noisy network of Rothe and Dahlke,⁷ and a cascade of noisy two-port networks.

If the Q vector is expressed in terms of Rothe and Dahlke's equivalent noise resistance r_n , equivalent noise conductance g_n , and complex correlation impedance Z_{cor} , we obtain

$$Q = 4kT_0\Delta f g_n \begin{pmatrix} \frac{r_n}{g_n} + |Z_{\text{cor}}|^2 \\ Z_{\text{cor}} \\ Z_{\text{cor}}^* \\ 1 \end{pmatrix} \quad (5)$$

³ H. Poincaré, "Mémoire sur les groupes Kleinéens," Acta Mat., vol. 3, pp. 49-92; 1883.

⁴ E. Picard, "Sur un groupe de transformations des points de l'espace situés du même côté d'un plan," Bull. Soc. Math. Franc., vol. 12, pp. 43-47; 1884.

⁵ R. Fricke and F. Klein, "Vorlesungen über die Theorie der automorphen Functionen," B. G. Teubner Verlag, Leipzig, Germany, vol. 1; 1897.

⁶ E. F. Bolinder, "Theory of noisy two-port networks," presented at the URSI-IRE meeting, Washington, D. C.; April 23-26, 1958.

⁷ H. Rothe and W. Dahlke, "Theory of noisy four-poles," Proc. IRE, vol. 44, pp. 811-818; June, 1956; "Theorie rauschender Vierpole," Arch. Elekt. Überw., vol. 9, pp. 117-121; March, 1955.

where k is Boltzmann's constant, T_0 is the absolute temperature, and Δf is the bandwidth.

A complete presentation of the geometric-analytic theory of noisy two-port networks will be given elsewhere.

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Comparison of Phase Difference and Doppler Shift Measurements for Studying Ionospheric Fine Structure Using Earth Satellites*

In using signals from earth satellites to investigate ionospheric fine structure, it would appear that at least two approaches might be used. One is the technique of measuring continuously the phase difference of signals received over slightly different paths (spaced receiving antennas), and the second is that of examining the Doppler shift on the frequency of a single signal.

The basic differences in the two techniques can be best illustrated by neglecting terms due to gross geometrical effects (which can be eliminated in the recording process by a number of techniques). In Fig. 1, two antennas spaced by a distance Z receive signals from source S . The propagation medium is considered essentially constant except for a region whose thickness is small compared to the height H of the source.

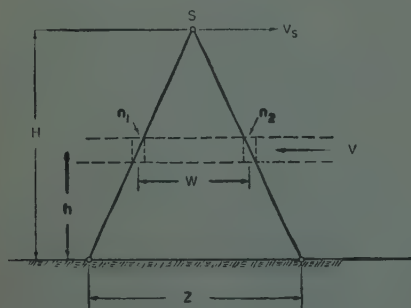


Fig. 1—Simplified geometry for phase difference measurements.

(This assumption is included mainly to permit considering the two rays as parallel during their transit through the layer.) The motion of the source is now replaced by assuming a velocity V of the layer.

The phase difference between the two signals is:

$$\alpha(\pi) = \phi_1 - \phi_2 = \frac{2\pi L}{\lambda_0} (n_1 - n_2).$$

The geometric paths, L , are considered of equal lengths, and n_1 and n_2 are the effective refractive indexes for the two rays in the layer.

If we consider one component of the index structure

$$n_i = A_i \sin k_i x, \quad \left(k_i = \frac{2\pi}{\lambda_i}\right)$$

in terms of the assumed layer velocity V , the time variation of α will be

$$\alpha_i(t) = \frac{2\pi L}{\lambda_0} A_i [\sin \omega_i t - \sin \omega_i (t + \tau)]$$

where

$$\omega_i \tau = \frac{2\pi W}{\lambda_i} \quad \text{and} \quad W = Z \left(1 - \frac{h}{H}\right).$$

Removing the time function $\sin \omega_i t$, this may be written as

$$\begin{aligned} \alpha_i &= \frac{2\pi L}{\lambda_0} A_i 2 \sin \frac{\omega_i \tau}{2} \\ &= \frac{2\pi L}{\lambda_0} A_i 2 \sin \frac{\pi W}{\lambda_i} \end{aligned} \quad (1)$$

indicating that such recordings of phase difference are insensitive to certain discrete wavelengths in the medium depending upon the antenna spacing and other geometry. That is, for any wavelength λ_p for which W/λ_p is integral, the quantity α will not contain a contribution from A_p .

To examine the similar property of the Doppler frequency shift, we differentiate, with respect to time, the phase of the signal received at one antenna. Thus

$$\begin{aligned} \Delta f &= \frac{1}{2\pi} \frac{d}{dt} \left[\frac{2\pi L}{\lambda_0} n \right] \\ \Delta f &= \frac{L}{\lambda_0} \frac{dn}{dt}. \end{aligned}$$

Again, examining the contribution of i th component and replacing x by Vt , we obtain:

$$\begin{aligned} \Delta f &= \frac{L}{\lambda_0} A_i k_i V \cos k_i Vt \\ &= \frac{L}{\lambda_0} A_i \frac{2\pi V}{\lambda_i} \cos \omega_i t. \end{aligned}$$

Removing the time function $\cos \omega_i t$, this becomes

$$\Delta f = \frac{2\pi L}{\lambda_0} A_i \frac{V}{\lambda_i} \quad (2)$$

indicating that in the limit of very long wavelengths in the index structure (λ_i) and in the case of zero velocity of the layer (V) the Doppler produces no information concerning the amplitude A_i of the i th component. However, (2) states that the "sensitivity" is inversely proportional to the wavelength λ_i and thus becomes greater for shorter components. This, of course, is very desirable from the standpoint of fine structure experiments.

Fig. 2 plots both (1) and (2) for comparison. The added scale on the abscissa is based on an assumed physical situation to indicate the order of the effects expected in the case of a satellite.

The clearly defined minima predicted in the phase records are not seen in similar

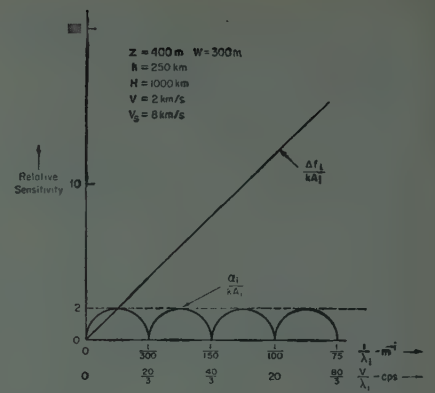


Fig. 2—Relative response of phase difference and Doppler measurements to different spatial wavelengths of ionospheric turbulence for simplified case.

measurements in the troposphere¹ and would not actually be expected for the ionosphere. This may be interpreted as indicating that the turbulence occurs throughout a sufficient range of the paths so that the superposition of many effective values of W results in smoothing out the nulls indicated for the simple case.

An important practical consideration in comparing the two approaches is the frequency stability of the satellite transmitter. In the observations of phase difference, frequency variations do not enter as a first-order effect. In contrast, since the Doppler measurements are primarily a frequency measurement, fluctuations in transmitter frequency are indistinguishable from the ionospheric effects to be measured.

The foregoing is intended only as a preliminary consideration because the final practical answer as to what technique is more desirable in a given case depends upon additional factors, such as the actual performance available in instruments for measuring phase differences and frequency differences.

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¹ J. W. Herbstreit and M. C. Thompson, Jr., "Measurements of the phase of radio waves received over transmission paths with electrical lengths varying as a result of atmospheric turbulence," *Proc. IRE*, vol. 43, pp. 1391-1401; October, 1955.

AM Transmitters As SSB Jammers*

In recent months much has been written concerning the advantages of using SSB in preference to AM for radiotelephone service. Power comparisons which have been made between these two systems have yielded a variety of decibel gain figures in favor of SSB. It is quite apparent that if one is skilled at making assumptions, decibel gain

* Received by the IRE, June 2, 1958.

* Received by the IRE, June 2, 1958.

figures suitable for almost any occasion may be obtained. It is pointless to debate this issue since the calculations are almost always correct leaving only the assumptions (which are a matter of personal judgment) as the subject for controversy.

While it must be conceded that a suppressed-carrier SSB system will generally show a power gain when compared with an equivalent AM system in a communications circuit, a rather dramatic change takes place when the AM transmitter is used as a jammer *against* the SSB transmitter. It is my purpose here to demonstrate that an AM transmitter, if properly used, can be quite effective as an SSB jammer.

For purposes of discussion let us assume that we are to jam a 1-kilowatt (peak envelope power output) suppressed-carrier SSB transmitter and that we are given a 125-watt (carrier output) AM transmitter with which to do the job. Antenna gains and propagation conditions for both the SSB and AM units must be chosen as identical. Now, how do we use the AM transmitter and what degree of success may we expect in our efforts to jam the SSB circuit?

The answer to the first part of this question is quite simple. Since the SSB receiver responds to RF signals in a band extending from, let us say, 300 to 3000 cycles away from the SSB carrier frequency, we must set the AM jammer frequency and choose a form of modulation for the AM transmitter which will produce the highest possible average RF power in this 2700-cycle pass band. Thus, we set the AM carrier frequency in the center of the SSB pass band (1650 cycles away from the SSB carrier frequency) and modulate with a square wave of fundamental frequency, say, 100 cycles and upper frequency limit of 1350 cycles. Such a square wave will be sufficiently "square" to yield very nearly 125 watts of average sideband power and together with the 125 watts of average carrier power we will have a total of 250 watts of average jamming power falling in the SSB pass band. (Perhaps a more direct way of arriving at this result is to visualize the jammer signal in the time domain. With square-wave modulation we have no output half of the time and twice the carrier voltage level the other half of the time. Thus, we have 500 watts being radiated with a 50 per cent duty cycle yielding 250 watts of average power.)

In order to estimate the degree of success which may be expected with our available 250 watts of average jamming power, we must determine the average sideband power which will result from speech modulation of the 1-kilowatt SSB transmitter. Admittedly, any choice for the peak-to-average power ratio for voice SSB that we may make will be subject to challenge. If one attempts to pick a mean of the figures which have been published, a four-to-one ratio would probably be a reasonable one. In other words, an SSB transmitter having one kilowatt of peak-power capability will radiate an average power of 250 watts when voice modulated. Thus, we see that the 125-watt AM transmitter can be quite effective as an SSB jammer since its use can result in a signal-to-jamming average power ratio of unity at the output terminals of the SSB receiver.

The situation outlined above is quite significant, not only because of the power ratios but also because of the cost ratios which are involved. What defensive measures does SSB then offer against this type of jamming? There are perhaps two types of action which may be taken by the SSB operators, neither of which offers an effective solution. First, the obvious (and that is the trouble) thing to do is to switch sidebands when jammed. This requires some coordination between transmitter and receiver and in addition such action will be expected and carefully watched for by the jammer. When we realize that "changing sidebands" in SSB is equivalent to changing the operating frequency we see that SSB offers no special advantage in this regard. Secondly, a narrow-band rejection or "notch" filter could be installed in the SSB receiver to take out the AM carrier heterodyne. In the case cited above, such action would cut the jammer's effectiveness by two-to-one in average power or 3 db. However, such tunable filters are seldom employed in SSB receivers outside the amateur field, probably because of the skill and attention which is required of the operator for satisfactory results. (On the other hand, without such filters the SSB system becomes quite vulnerable to straight continuous-wave jamming; a situation which makes the communications equipment-to-jamming equipment cost ratio even larger.) Although one might wish to argue the details of what is given above, the basic premise that an AM transmitter can be quite effective as a jammer against SSB seems secure.

In closing, it is somewhat interesting to observe that in the previous example a signal-to-jamming average power ratio of unity, or zero db, at the output of the receiver was obtained by using a 125-watt AM transmitter against a 1-kilowatt SSB transmitter. I shall resist the temptation of computing the AM power advantage in decibels.

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Taper Sections in Circular Waveguides*

Solymar¹ has discussed the determination of the TE_{0n} modes distribution produced by a conical tapered transaction between two circular waveguides.

In the writer's doctorate dissertation in electrical engineering² the same structure, among other problems, was considered. The problem was approached in a different manner but the results obtained were essentially the same as those obtained by Solymar.

* Received by the IRE, June 2, 1958.

¹ L. Solymar, "Design of a conical taper in circular waveguide system supporting H_{01} mode," *Proc. IRE*, vol. 46, pp. 618-619; March, 1958.

² G. Gerosa, "Study of a very long feeding system for a microwave lens aerial using a circular waveguide propagating TE_{01} mode," Electrotechnical Institute, University of Rome, Italy; March 31, 1956.

The field in the tapered section has been represented as superposition of modes of the cylindrical guide and the generalized telegraphist's equations³ have been derived. The TE_{01} mode is found to be coupled only with TE_{0n} modes. The coupling is expressed by the voltage and current transfer coefficients which decrease as n increases.

Assume the following:

- 1) structure without losses,
- 2) cone of small aperture,
- 3) diameters of the two guides to be connected not very different and much larger than the cutoff diameters for the TE_{01} and TE_{02} modes,
- 4) only first-order approximation considered,
- 5) reflections at the junctions at the tapered section neglected,
- 6) all the energy carried by the TE_{01} mode in the input guide.

For the excitation of the TE_{02} mode a formula practically identical to the one given by Solymar is obtained; the only difference is that in place of the factor a/λ there is the factor $(a+b)/2(\lambda_{01}\lambda_{02})^{1/2}$ where a and b are the radii of the two guides and λ_{01} and λ_{02} , the wavelengths for the TE_{01} and TE_{02} modes in a guide of radius $(a+b)/2$.

It may not be out of place here to mention that using the telegraphist's equations approach to calculate the variation of the propagation constants due to the imperfect conductivity of the walls and the mode conversion due to curves in the circular guides, the writer² has found results essentially identical with those obtained by Oswald⁴ and Jougeut,⁵ who used a different approach.

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³ S. A. Schelkunoff, "Conversion of Maxwell's equations into generalized telegraphist's equations," *Bell Sys. Tech. J.*, vol. 34, pp. 995-1043; September, 1955.

⁴ J. Oswald, "Calcul des pertes par effet joule dans les guides d'ondes," *Cables & Transm.*, vol. 1, pp. 205-219; October, 1947.

⁵ M. Jougeut, "Les effets de la courbure sur la propagation des ondes électromagnétiques dans les guides à section circulaire," *Cables & Transm.*, vol. 1, pp. 133-153; July, 1947.

Common Emitter Transistor Amplifiers*

The recent letter from Dion¹ pointing out the equivalence of an emitter follower and a common emitter amplifier with resistance in series with the base is interesting. There is, however, a further point that should be considered: the gain stability in the two cases.

As has been shown,² the gain stability of a transistor amplifier depends upon the re-

* Received by the IRE, June 16, 1958.

¹ D. F. Dion, "Common emitter transistor amplifiers," *Proc. IRE*, vol. 46, p. 920; May, 1958.

² R. F. Purton, "Transistor amplifiers: common base versus common emitter," *ATE J.*, vol. 14, pp. 157-163; April, 1958.

distances in series with its electrodes. The most variable transistor parameter both from unit to unit and with respect to frequency and ambient variations is probably α_{fe} . The power gain stability against variation in α_{fe} is improved by resistance in series with the emitter (emitter feedback), but is worsened by resistance in series with the base. The emitter follower arrangement is, therefore, preferable on this account.

The stabilities can be calculated as follows. If it is assumed that the input resistance is arranged to match the source resistance, then the circuits for the two cases are as shown in Fig. 1, with

$$R_G = R + R'_{IN} = \alpha_{fe} R_L \quad (1)$$

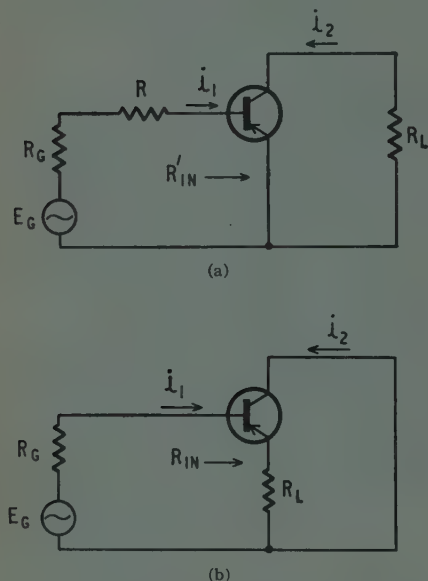


Fig. 1—(a) Common emitter amplifier with input resistance increased by addition of R . (b) Emitter follower amplifier.

For the common emitter amplifier, transducer power gain is

$$\begin{aligned} G_1 &= \alpha_{fe}^2 i_1^2 R_L \cdot \frac{4R_G}{E_G^2} \\ &= \alpha_{fe}^2 \cdot \frac{E_G^2 \cdot R_L}{(R_G + R + R'_{IN})^2} \cdot \frac{4R_G}{E_G^2} \\ &= \frac{4R_L R_G}{(R_G + R + R'_{IN})^2} \cdot \alpha_{fe}^2 \end{aligned} \quad (2)$$

Therefore, from (1), $G_1 = \alpha_{fe}$ as shown by Dion. Also, from (2),

$$\frac{dG_1}{G_1} = \frac{2\alpha_{fe} d\alpha_{fe}}{\alpha_{fe}^2} = \frac{2d\alpha_{fe}}{\alpha_{fe}} \quad (3)$$

i.e., a given percentage change in α_{fe} will produce twice this change in G_1 .

For the emitter follower

$$\begin{aligned} G_2 &= \alpha_{fe}^2 \cdot \frac{E_G^2 \cdot R_L}{(R_G + \alpha_{fe} R_L)^2} \cdot \frac{4R_G}{E_G^2} \\ &= \frac{4R_L R_G}{(R_G + \alpha_{fe} R_L)^2} \cdot \alpha_{fe}^2 \end{aligned} \quad (4)$$

Therefore again from (1) $G_2 = \alpha_{fe}$. From (4)

$$\frac{dG_2}{G_2} = \frac{2R_G}{(R_G + \alpha_{fe} R_L)} \cdot \frac{d\alpha_{fe}}{\alpha_{fe}}$$

Therefore from (1)

$$\frac{dG_2}{G_2} = \frac{d\alpha_{fe}}{\alpha_{fe}}$$

That is, the gain variation is only half that of the previous case.

It should be noted that both stabilities are poor—at least as bad as α_{fe} itself. This is because of the high source resistance in series with the base.

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Resonance-Probability and Entropy-Evolution Relationships*

RESONANCE-PROBABILITY

For some time now I have had the intuitive feeling that the Q of a tuned circuit, and the σ (standard deviation) of a probability distribution are close kin. Resonance curves seem to be a special class of probability curves. If so, there should be a whole family of analogies, whereby the many probability concepts have a running mate in an ac tuned circuit arrangement. In plain words, is there a basic underlying concept that covers both resonance effects and probability response? I think so, but so far I can't prove it. If ac circuits behavior is truly analogous to probability response, then ac circuits can provide a simple solution of complex problems in probability and statistics.

I have never found anything in the literature on the similarities between ac circuit response and probability. Just what is the probability counterpart of frequency? Of inductance? Of capacitance? Of resistance? Of Q ? Does any one know? Is it worth following up?

ENTROPY-EVOLUTION

The second concept that has disturbed my sleep of late is, what appears to me to be the amazing "face" correlation between cybernetic *entropy*, and organic evolution. Whereas thermodynamics uses *entropy* as an index of the unavailability of heat, cybernetics uses *entropy* in a broader sense: an index of the state of disorganization in any "system," be it organic, mechanical, or even semantic. Cybernetics shows that any state of organization tends toward disorganization; there is a natural tendency for order to downgrade toward disorder, that is, *entropy*, the index of disorder, always tends to increase.

Now, natural evolution is the process by which increased organization takes place; greater specialization results in time. More or less random variations fall into specialized patterns, which continue. So evolution is anti-entropic. The trend is from the scrambled to the organized; the ordered; the specialized.

In most cases, "nature" dictates that every state of organization tends toward breakdown, whether gradually or fast. In some unique cases, this apparent universal rule has the opposite polarity. From chaos, order and system sets in. It seems to me that "normal" cybernetic entropy and "normal" organic evolution are one and the same; except that entropy works in a + direction (toward breakdown) when cybernetics is considered, and in a - direction (toward improvement) when evolution is considered.

What I want to know is, what factors determine whether a "system" (machine or living thing) tends to breakdown or to build up? If we knew, then machines could be designed that have capabilities to improve their mode of operation as they work.

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The Dependence of Minority Carrier Lifetime on Majority Carrier Density*

In a recent letter Chang¹ has derived a simple relationship between the ratio of the diffusion length of holes in an n region to that of electrons in an adjacent p region and the ratio of the conductivities of the regions. This derivation was based on the assumption that the minority carrier lifetime is inversely proportional to the majority carrier density. This is only true under certain conditions which are discussed below.

We shall confine our attention to the semiconductors for which it has been shown that the recombination process can be described by the statistics of Shockley and Read,² viz., germanium³ and silicon.^{4,5} The low-level lifetime of the minority carriers, assuming a small density of recombination centers with a single recombination level, for the four possible cases which can arise is shown in Table I. τ_n and τ_p are the lifetimes of electrons and holes as minority carriers. τ_{no} is the lifetime of electrons injected into a highly p -type specimen; τ_{po} is the lifetime of holes injected into a highly n -type specimen. n_0 and p_0 are the thermal equilibrium electron and hole densities; n_1 and p_1 are the values the electron and hole densities

* Received by the IRE, June 9, 1958. This note is published by permission of the Dir. of Radio Res. of the Dept. of Sci. and Indus. Res., Eng.

¹ S. A. Chang, "Relation between ratio of diffusion lengths of minority carriers and ratio of conductivities," *Proc. IRE*, vol. 45, pp. 1019-1020; July, 1957.

² W. Shockley and W. T. Read, "Statistics of the recombinations of holes and electrons," *Phys. Rev.*, vol. 87, pp. 835-842; September 1, 1952.

³ J. A. Burton, et al., "Effect of nickel and copper impurities on the recombination of holes and electrons in germanium," *J. Phys. Chem.*, vol. 57, pp. 853-859; November, 1953.

⁴ G. Bemsli, "Lifetime of electrons in p -type silicon," *Phys. Rev.*, vol. 100, pp. 523-524; October 15, 1955.

⁵ C. A. Bittmann and G. Bemsli, "Lifetime in pulled silicon crystals," *J. Appl. Phys.*, vol. 28, pp. 1423-1426; December, 1957.

* Received by the IRE, April 25, 1958; revised manuscript received, June 26, 1958.

TABLE I

E_R in Upper Half of Energy Gap		E_R in Lower Half of Energy Gap	
Case 1: p -type	Case 2: n -type	Case 3: p -type	Case 4: n -type
$\tau_n = \tau_{n0} + \tau_{p0}n_1/p_0$ Provided that: for silicon $(E_F - E_V) \geq (E_C - E_R)$ or germanium $(E_F - E_V) > (E_C - E_R)$ by more than $3\frac{1}{2} kT$ then $\tau_n \approx \tau_{p0}n_1/p_0^*$	$\tau_p = \tau_{p0}(1 + n_1/n_0)$ Provided that: $(E_R - E_F) > 0$ by more than $1\frac{1}{2} kT$ for both silicon and germani- um then $\tau_p \approx \tau_{p0}n_1/n_0^*$	$\tau_n = \tau_{n0}(1 + p_1/p_0)$ Provided that: $(E_F - E_R) > 0$ by more than $1\frac{1}{2} kT$ for both silicon and germani- um then $\tau_n \approx \tau_{n0}p_1/p_0^*$	$\tau_p = \tau_{p0} + \tau_{n0}p_1/n_0$ Provided that: for silicon $(E_C - E_F) > (E_F - E_V)$ by more than $3 kT$; for germanium $(E_C - E_F) \geq (E_F - E_V)$ then $\tau_p \approx \tau_{n0}p_1/n_0^*$

* The above inequalities are based on a maximum error in the approximation of about 25 per cent.

TABLE II

	Case 3: p -type		Case 4: n -type	
	$(E_R - E_V)$ in ev	Resistivity in ohm-cm	$(E_R - E_V)$ in ev	Resistivity in ohm-cm
Germanium	0.048 ^a 0.27 ^b 0.27 ^c	>0.02 >6 Invalid*	0.27 ^b 0.27 ^c	>0.3 >5
Silicon	0.065 ^{a†} 0.09 [‡] 0.14 [‡] 0.17 [‡] 0.24 [‡]	>0.1 >0.3 >2 >6 >20	0.055 ^{a†} , 0.063 [‡] , 0.067 [‡] 0.14 [‡] 0.175-0.19 [‡] 0.225-0.24 [‡]	>0.02 >0.05 >20 >125

* The expressions for the minority carrier lifetime in Table I apply only to extrinsic material.

† In transistors.

‡ In diodes.

would have if the Fermi level were located at the same position in energy as the recombination centers. The energy level of the recombination centers is denoted by E_R , the thermal equilibrium position of the Fermi level being denoted by E_F . Fig. 1 shows the position of the Fermi level, as a function of resistivity in germanium and silicon. The values for the mobilities were taken from the published literature and the densities of states were calculated using effective masses determined from cyclotron resonance data, viz., $M_e = 0.55M_0$, $M_h = 0.37M_0$ for germanium; $M_e = 0.27M_0$, $M_h = 0.39M_0$ for silicon.

Fig. 1 shows the location of the main recombination levels in germanium and silicon. These levels have been attributed to the presence of copper atoms. All the recombination levels are shown in the lower half of the energy gap since the published literature suggests that this is the case. It is assumed in Table I that τ_{n0} is about ten times τ_{p0} for germanium,³ and that τ_{p0} is nine times τ_{n0} for silicon.⁵

It can be seen from Table I and Fig. 1 that the general requirement for the assumption that the minority carrier lifetime is inversely proportional to the majority carrier density to be valid is, in all four cases, that the recombination levels lie near the appropriate band edge and/or that the

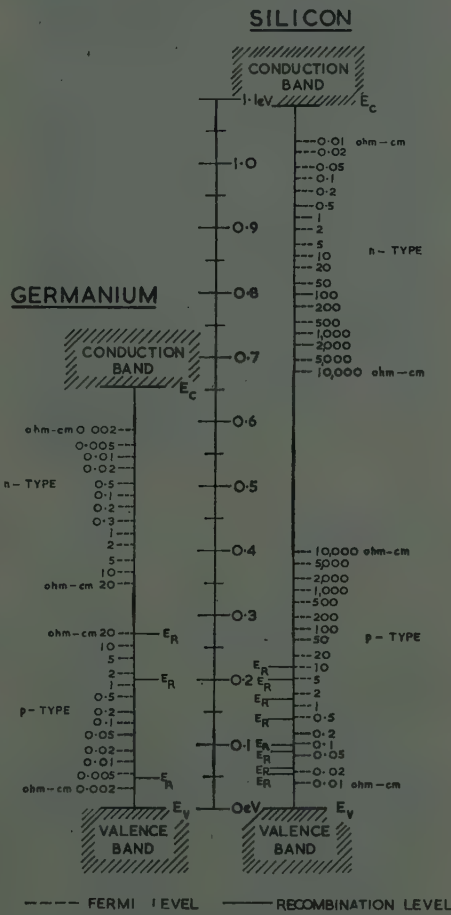


Fig. 1—Energy levels in germanium and silicon at 300°K.

semiconductor should be only weakly extrinsic.

Table II, relating to cases 3 and 4, which are those of interest, shows the resistivity ranges for which the assumption is valid for the main recombination levels reported for germanium and silicon.

In Table II, for the recombination levels shown in the first two lines for n -type silicon, it is assumed that τ_{n0} is $2.75\tau_{p0}$.³

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The Internal Current Gain of Drift Transistors*

For diffusion-type (homogeneous-base) transistors the common-base internal short-circuit current gain α_d can be specified in terms of two parameters. These are f_{ad} , its internal cutoff frequency, and α_{d0} , its zero-frequency value,¹ both of which depend on a single dimensionless parameter $\omega W^2/2D$ (for a unidimensional model). Here ω is the angular frequency, W the active base width of the transistor, and D the diffusion constant for minority carriers in the base. For drift (inhomogeneous-base) transistors this is no longer the case, because the value of α_d depends in effect on two dimensionless parameters $\omega W^2/2D$ and $\Delta V/kT$; the latter is the relative drift potential across the base.

Although measurements of the external complex current transmission under finite termination conditions are possible,^{2,3} and from these the internal complex current gain may be determined, such measurements involve specialized and costly equipment, which is not always readily available. The purpose of the present note is to show that a complete specification of the internal current gain of a drift transistor can be obtained using a relatively simple method.

If the complex theoretical loci of α_d are calculated from Kroemer's theory,⁴ in terms of $\omega W^2/2D$ and $\Delta V/kT$, which may be regarded as disposable parameters,⁵ it is found that there is a direct relationship between the ratio f_{ad}/f_1 and $\Delta V/kT$, where f_1 is the frequency at which the modulus of the common-emitter internal short-circuit current gain β has a value of unity.⁶ This relationship is shown in Fig. 1 for values of $\Delta V/kT$ up to eight. It is clear, therefore, that for such practical drift transistors as conform to the theoretical model, we may determine $\Delta V/kT$

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¹ R. L. Pritchard, "Frequency variations of current amplification factor for junction transistors," *Proc. IRE*, vol. 40, pp. 1476-1481; November, 1952.

² F. J. Hyde and R. W. Smith, "An investigation of the current gain of transistors at frequencies up to 150 mc/s," *Proc. IEE*, vol. 105B, pp. 221-228; 1958.

³ H. G. Follingstad, "Complete linear characterization of transistors from low through very high frequencies," *IRE TRANS. ON INSTRUMENTATION*, vol. I-6, pp. 49-63, March, 1957.

⁴ H. Kroemer, "The drift transistor," in "Transistors I," RCA Labs., Princeton, N. J., p. 202; 1956.

⁵ F. J. Hyde, "An investigation of the current gain of a drift transistor at frequencies up to 105 mc/s," *Proc. IEE*, to be published.

⁶ In a private communication from L. G. Cripps, it was shown that f_1 is also the frequency at which the real part of α_d has a value of $\frac{1}{2}$.

^a M. S. Rideout, "The Temperature Dependence of Minority Carrier Lifetime in p -Type Germanium and Silicon," Rep. of the Meeting on Semiconductors (Physical Society and B.T.H., Ltd., Rugby, England), pp. 33-37; April, 1956.

^b R. G. Shulman and B. T. Wyluda, "Copper in germanium: recombination center and trapping center," *Phys. Rev.*, vol. 102, pp. 1455-1457; June 15, 1956.

^c D. M. Evans, "The measurement of the temperature dependence of the mobility and effective lifetime of minority carriers in the base region of silicon transistors," to be published.

^d B. Ross and J. R. Madigan, "Thermal generation of recombination centres in silicon," *Phys. Rev.*, vol. 108, pp. 1428-1433; December 15, 1957.

^e D. J. Sandiford and J. Shields, "Reverse Currents and Carrier Lifetimes in Silicon p - n Junctions," Rep. of the Meeting on Semiconductors (Physical Society and B.T.H., Ltd., Rugby, England), pp. 49-54; April, 1956.

^f D. M. Evans, unpublished.

TABLE I
CURRENT GAIN DATA OF COMMERCIAL DRIFT TRANSISTORS

Transistor		2N247 No. 1	2N247 No. 2	2N247 No. 3	2N247 No. 4	2N384
Measured f_{α} , mc		40	35	41.5	43	92.5
Measured f_{β} , mc		24	20	26.5	26.5	50
f_{α}/f_{β}		1.67	1.75	1.57	1.62	1.85
ΔV	From above value of f_{α}/f_{β}	5.0	5.75	4.0	4.5	6.75
kT	From analysis of complex α and α_d	5.0	5.5	4.0	4.0	7.0
Measured values of c_e , pF		100	50	80	80	35
$\omega c_e r_e'$ at $I_e=2.0$ ma		0.31	0.14	0.26	0.27	0.25

from the ratio f_{ad}/f_1 . If α_{d0} , f_{ad} , and $\Delta V/kT$ are known, then α_d may be specified at any frequency, by fitting the data to a family of universal curves for α_d .⁵

Now in practice f_{ad} and f_1 cannot be measured directly because they are "internal" parameters. We may readily measure the corresponding external parameters, however, which will be designated f_{α} and f_{β} , respectively. The effects of the ohmic base resistance r_{bb}' and collector depletion-layer capacitance c_c on the relationships between f_{α} and f_{ad} and between f_1 and f_{β} are small for the drift transistor.⁵ That of the emitter depletion-layer capacitance c_e can be made small by operating at a high value of direct emitter current I_e . Too high a value of I_e , however, will give rise to high-level injection and heating effects which should be avoided.

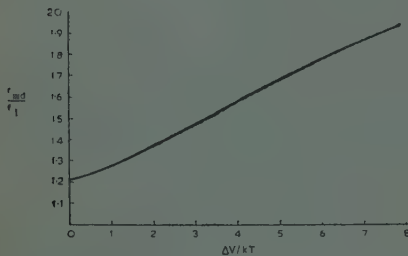


Fig. 1—Dependence of the ratio f_{ad}/f_1 on $\Delta V/kT$.

Provided that the dc operating condition is suitably chosen, we may then use the ratio f_{α}/f_{β} instead of f_{ad}/f_1 to determine $\Delta V/kT$ from Fig. 1. The extent of the approximation involved in ignoring the effect of c_e may be estimated from (1), which shows the relationship between the measured near-short-circuit external current gain α and α_d as affected by c_e ,

$$\alpha_d = \alpha(1 + j\omega c_e/y_i). \quad (1)$$

Here y_i is the internal short-circuit emitter input admittance for the common-base connection, and is complex. It may be calculated from theory using data obtained from low-frequency measurements⁵ of β , or to a first approximation it may be replaced by $1/r_e'$ where r_e' is given by $25/I_e$ ohms when I_e is in milliamperes. c_e may be measured by one of several methods to be described in a later publication. The condition required for $f_{\alpha} \approx f_{ad}$ and $f_{\beta} \approx f_1$ is that $\omega c_e r_e' \ll 1$ at the frequencies in question. The condition for f_{α}/f_{β} to be approximately equal to f_{ad}/f_1 is less stringent, because ratios are involved

and the corrections to f_{α} and f_{β} to obtain f_{ad} and f_1 , respectively, are both in the same sense. Results are presented in Table I for four 2N247-type transistors ($I_e = 2.0$ ma, $V_c = -9.0$ volts) and one 2N384-type transistor ($I_e = 2.0$ ma, $V_c = -12$ volts). The values of $\Delta V/kT$ in the fourth row have been determined from the ratio f_{α}/f_{β} and Fig. 1. Those in the fifth row have been obtained from a detailed analysis of the loci of the complex external current gain,⁵ which were measured by a twin-channel comparator method² in the frequency range 1–105 mc. The two sets of data are seen to be in good agreement.

In the penultimate row the values of emitter depletion-layer capacitance are shown and in the last row, the values of $\omega c_e r_e'$. From these values it may be estimated that the ratio f_{α}/f_{β} should not differ greatly from f_{ad}/f_1 .

The internal consistency of the results is such as to suggest that the transistor types investigated conform to Kroemer's simple model and that the value of $\Delta V/kT$ and hence α_d at any frequency may be readily determined.

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Theory of Diode and Transistor Noise*

The representation of noise in junction diodes and transistors above the 1/f range by superposition of a thermal noise source (Nyquist) and a current generator (Schottky noise source) has recently been used extensively.¹⁻³

The theory is based upon independent

* Received by the IRE, May 27, 1958.

¹ A. van der Ziel and A. T. Becking, "Theory of junction diode and junction transistor noise," *Proc. IRE*, vol. 46, pp. 589–594; March, 1958.

² A. Uhlir, "High-frequency shot noise in $p-n$ junctions," *Proc. IRE*, vol. 44, p. 557; April, 1956, correction, p. 1541; November, 1956.

³ W. Guggenbühl and M. J. O. Strutt, "Theorie des Hochfrequenzrauschens von Transistoren bei kleinen Stromdichten," *Nachrichtentechn. Fachberichte*, vol. 5, pp. 30–33; 1956.

W. Guggenbühl and M. J. O. Strutt, "Theory and experiments on shot noise in semiconductor junction diodes and transistors," *Proc. IRE*, vol. 45, pp. 839–854; June, 1957.

carrier motion and one-dimensional diffusion process:

$$D_p \frac{\partial^2 p}{\partial x^2} = \frac{\partial p}{\partial t} - \frac{p - p_n}{\tau_p} \quad (1)$$

with $(p - p_n)$ = excess-hole concentration (p_n = equilibrium concentration), τ_p = lifetime, and D_p = hole-diffusion constant.

Using the transmission line analogy or other formalism, the following equation for the noise current can be derived:

$$\bar{i}^2 = 4kTGdf - 2eIdf \quad (\text{usual notations}) \quad (2)$$

with G = junction conductance, I = junction current (positive for forward, negative for backward bias).

The assumptions in this case exclude, e.g., high-current regions or a more complicated geometry as in the case of point-contact diodes.⁴

It might be interesting to note that a similar representation was used years ago for point-contact devices.⁴ The difference was, roughly speaking, based on the assumption of a shot-noise current uncorrelated and additive to the Nyquist noise of the differential resistance. This leads to

$$\bar{i}^2 = 4kTG\Delta f + 2e|I|df. \quad (3)$$

$|I|$ = absolute current value in both directions.⁴

This expression can be derived on the basis of an equivalent network for a barrier with an exponential current-voltage relation of the form $I_f = kV^n + pV$, and was based on noise-factor measurements on many of the available point-contact diodes (Ge and Si). A law for the dynamic case was also derived which was especially useful for the mixer case;⁵ the equivalent dynamic noise factor, p , which correlates the diode noise to the Nyquist noise of the differential resistance, is

$$p(\theta) = A + \frac{20}{\pi} V \left[\frac{n+1}{n} \sin \theta + \left(\pi - \frac{n+1}{n} \theta \right) \cos \theta \right] \quad (4)$$

when V = exploration voltage, A = constant, n = exponent of characteristic, and θ = angle of current flow.

The higher noise current of point-contact diodes, and the deviations of the $I(V)$ characteristics from the Schottky-Wagner form⁶

$$I = I_0(e^{\alpha V} - 1)$$

with $\alpha = 40$ volts⁻¹ are considered in the multi-contact theory⁷ which made it necessary to assume uncorrelated noise contributions as in (3). In this case the semiconductor noise

⁴ H. F. Mataré, "Das Rauschen von Dioden und Detektoren im statischen und dynamischen Zustand," *Elek. Nach. Tech.*, vol. 19, pp. 111–126; 1942. "Bruit de fond des diodes à cristal," *Onde élect.*, vol. 29, pp. 231–240; June, 1949, and "Statistische Schwankungen in Halbleitern," *Z. Naturf.*, vol. 4, pp. 275–283; 1949.

⁵ H. F. Mataré, "Bruit de fond de semiconducteurs I," *J. Phys. Radium*, vol. 8, pp. 364–372; December, 1949, and "Bruit de fond de semiconducteurs II," vol. 11, pp. 130–140; March, 1950, "Empfangsprobleme im Ultrahochfrequenzgebiet," Verlag R. Oldenbourg, Munich, Ger.; 1951.

⁶ H. A. Bethe, "Theory of the boundary layer of crystal rectifiers," *RL Report No. 43-12*; November 23, 1942.

⁷ H. J. Vearian, "DC characteristics of silicon and germanium point contact crystal rectifiers," *Brit. J. Appl. Phys.*, vol. 21, pp. 187–221, and "The multi-contact theory, Part II," vol. 21, pp. 283–289, 1950.

can also be calculated on the basis of an appropriate equivalent network.⁴ This scheme was used later to calculate harmonics mixing and reinforcement with Ge and Si point-contact diodes.⁵

Apparently the approach used in (3) for junctions should be applied, for which the restrictive assumptions leading to (2) are not fulfilled, e.g., in the case of high-current densities (power devices) and more complicated contact geometries when the individual noise currents of parallel junctions are not correlated.

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* H. F. Mataré, "Oberwellenmischung und Verzerrung mit Kristalldioden," *Arch. elekt. Übertr.*, vol. 7, pp. 1-15; 1953.

Dispersion of High-Frequency Elastic Waves in Thin Plates*

In a recent application of the theory of elastic waves in thin plates to ultrasonic delay lines, Mapleton¹ has reviewed most of the mathematical phases of the problem.

On comparing his calculations with our own work, the following extension was derived which is of practical value. The primary problem in transmission of ultrasonic energy is to consider the effects of dispersion on the delay time and reproducibility of the pulse. It should be emphasized that the dispersion effects noted below are not intrinsic in the medium as in optical materials but are introduced by the boundary conditions.

The first solution of the shear waves discussed by Mapleton is of the most importance, and his frequency equation may be considerably simplified by suitable approximations. The first is $\Delta^2 = \beta^2 = k_T^2 - k^2$ to yield

$$4\alpha\beta k^2 \sinh(k\beta)$$

$$+ (\beta^2 - k^2) \tanh(\alpha h) \cos \beta h = 0. \quad (1)$$

On dividing through by k^4 and rearranging terms and eliminating β and α

$$\tan[\pi(2\psi\Delta - 1)/2\Delta]$$

$$= 4[1 - \xi(1 + \Delta^2)]^{1/2}/(1 - \Delta^2)^2$$

$$\cdot \coth \pi\psi[1 - \xi(1 + \Delta^2)]^{1/2} \quad (2)$$

where

$$\psi = \frac{2hf}{v} \quad \text{and} \quad \xi = \left(\frac{v_t}{v_L}\right)^2$$

and $2h$ =thickness of plate, f =frequency, and v =velocity of wave.

For the large values of the argument ψ , $\coth \psi$ approaches 1.00 as a limit; and with

the condition Δ is a small quantity, only relatively constant terms are on the right side of (2). For fused quartz, the constant H is 3.004, and since the tangent is a cyclic function with period π , successive values of Δ_n satisfying the transcendental equation may be had:

$$\tan \frac{1}{2}\pi[2\psi\Delta_n - (2n+1)/\Delta_n] = H$$

$$\text{where } n = 0, 1, 2, 3 \dots \quad (3)$$

As Δ_n is small, the tangent may be expanded: $\tan \psi = \psi + \psi^3/3! + \dots$ and only the first term retained.

$$\Delta_n = (n + \frac{1}{2})/\psi(1 - H/\psi\pi). \quad (4)$$

Now if $v/v_t = 1 + \delta$ from the expansion of β^2 , $\delta_n = \frac{1}{2}\Delta_n^2$

$$\delta_n = \frac{1}{2}[(n + \frac{1}{2})/(\psi - H/\pi)]^2$$

$$\text{and for } \psi \gg H/\pi \quad (5)$$

$$\delta_n \approx \frac{1}{2}[(n + \frac{1}{2})/\psi]^2$$

$$= \frac{1}{2}[(n + \frac{1}{2})v/2hf]^2. \quad (5a)$$

Eq. (5) will give the increment in velocity as a function of the order of the mode, frequency, and thickness of plate. The last term may be neglected in many cases as in (5a). Mapleton's frequency equation for the second solution of the shear wave has been similarly treated and gives the even modes in the plate. The compressional cases yield solutions identical in form with the shear cases. Calculations of δ_n based on (5) have agreed with Mapleton's values for the shear case, but plots on log-log papers of his other values against h do not give a straight line with -2 slope for the compressional modes in fused quartz and the single crystal calculations.

The analogy between the elastic vibrations in the plate and the electromagnetic modes in a wave guide is excellent, if more complicated, if it is recalled that Mapleton's work deals with phase velocity, and not the group velocity with which the energy of a pulse is transmitted. The latter turns out to be

$$v_0 = (\partial k/\partial \omega)^{-1} = C_T(1 - \delta_n). \quad (6)$$

Table I summarizes approximately the dispersion effects in a 1000- μ sec line, at 15 mc, 0.636 cm thick, using (5a).

TABLE I

Freq. mc	Delay Mode	Excess— μ sec			Number of Cycles Deficit		
	Mode	3	5		1	3	5
5	1.86	16.74	48.50		9.00	81	225
10	0.465	4.185	11.625		4.48	40.32	112
15	0.210	1.89	5.25		3.00	27.00	75.0
20	0.116	1.046	2.90		2.24	20.16	55.6
25	0.074	0.667	1.86		1.8	17.1	45.0
30	0.052	0.273	1.31		1.49	13.4	37.2
35	0.032	0.207	0.57		1.28	11.5	32.0

The practical significance of (5) or (5a) lies in the dispersion effects that will arise in thin plates used for wide band delay lines. At 15 mc, Table I shows an excess of 0.210 μ sec in the lowest mode and within the band pass from 10-20 mc that may be used for short pulses, the excess varies from 0.42 to 0.12, respectively. This would result in a distorted pulse with a steeper rise than fall.

Furthermore, although no consideration has been paid to the distribution of energy

in the different modes, it is evident that these can be excited and conflict with each other. A reasonable assumption might be that the amplitude in each mode after equilibrium has been reached varies as for plane wave excitation. Thus when comparable amounts of energy exist in the different modes, the differences in the cycles delayed should be evident with pass band measurements made under CW or pulsed conditions. Between 10 and 20 megacycles, the lowest two modes differ by 36 and 18 cycles, respectively, so that 18 maxima and minima between 3-8 db departure from a smooth curve in the 10-mc pass band are possible.

Effects of this type have been observed and agree well with the theory after reasonable allowances for other complicating factors are made.

The actual difference in velocity of the different modes may be observed in the longer lines at low frequency. For instance, a 2780 μ sec line one half inch thick gave a difference in rise time of 0.8 μ sec between 8 and 40 mc while throughout the pass band ripples spaced $\frac{1}{2}$ -1 mc apart were seen amounting to 6 db because of the phase relations in the modes. Even with short lines the dispersion effect is noticeable. Several 124 μ sec lines had ripples 6-8 mc wide superimposed on the band-pass of the crystal. By good design of crystal excitation and choice of line thickness as well as use of absorbing stops it is possible to suppress these ripples. Delay lines with less than $\frac{1}{2}$ -db ripple have been constructed in this laboratory.

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Computer Fabrication and Circuit Techniques*

Two techniques were developed during the design and construction of a small general purpose digital computer which may be of value to others working in this field. The first is a fabrication technique which obviates the need for super-conducting paths in the plug-in connectors. The control winding of a cryotron can be placed on the stationary unit, and a gate wire which is doubled back on itself to form a hairpin is placed on the plug-in unit. The gate wire acts as the pin and the control winding as the socket of a connector. Coupling between the two is magnetic, and therefore a super-conducting connection is not necessary. Information flow from the plug-in unit to the stationary unit requires that the control winding be on the plug-in unit and the gate hairpin on the stationary unit. The only ohmic contacts necessary are the power supply wires, the resistance of which is non-critical.

The second development is a circuit technique which forms a pulse on one of two

* Received by the IRE, June 25, 1958. This work was supported by the USAF through the Rome Air Development Center.

R. E. Mapleton, "Elastic wave propagation in solid media," *J. Appl. Phys.*, vol. 23, pp. 1346-1354; December, 1952.

* Received by the IRE, July 3, 1958.

wires to indicate a binary ONE or ZERO from a pulse-or-no-pulse representation on a single wire. In many logical circuits the output is frequently obtained in a pulse-or-no-pulse representation, while the two-wire complementary representation may be required by the inputs of the next logical circuit. The circuit described will provide the required conversion, as well as reduce the number of inputs from outside the helium bath. The circuit takes advantage of the ability of a cryotron to switch when a full-amplitude control current occurs and not switch when a half-amplitude control current occurs. The gate wires of two cryotrons are joined, and a pulse applied at the junction. One of the two cryotrons is always resistive. The other is resistive only when an input pulse occurs. The current therefore flows through a superconducting gate wire when no input pulse occurs, and divides equally between two resistive gates when an input pulse does occur. The current can then be routed to the control winding of one cryotron of a second pair of cryotrons in such a way that the cryotron is resistive only when no input pulse occurs. The other cryotron of the second pair of cryotrons therefore contains the information in complementary form.

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Radiometer Circuits*

In a recent letter to the editor¹ the least detectable noise for a number of radiometer circuits originally described in a previous article² was given as follows:

$$\begin{aligned}\sigma_{1d}^2 &= 4\sigma_n^2 \sqrt{\frac{\gamma}{\alpha}} && \text{sine wave modulation} \\ & && \text{sine wave multiplier} \\ \sigma_{1d}^2 &= \pi\sigma_n^2 \sqrt{\frac{\gamma}{\alpha}} && \text{square wave modulation} \\ & && \text{sine wave multiplier} \\ \sigma_{1d}^2 &= 2\sigma_n^2 \sqrt{\frac{\gamma}{\alpha}} && \text{two receiver cross} \\ & && \text{correlation.}\end{aligned}$$

The figure for square wave modulation and square wave multiplier was not given but would be

$$\sigma_{1d}^2 = \frac{8}{\pi} \sigma_n^2 \sqrt{\frac{\gamma}{\alpha}}.$$

An alternate system shown in Fig. 1 uses two receivers but one antenna. The signals $y_1(t)$ and $y_2(t)$ both contain receiver noise, which is assumed the same for both receivers. Since there is no correlation between

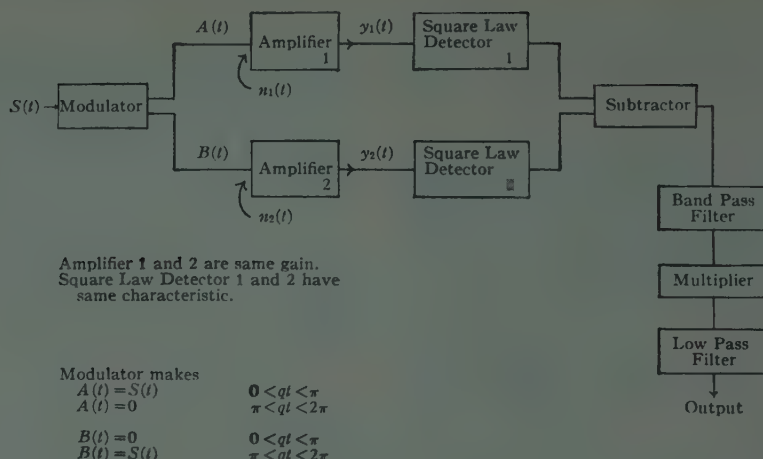


Fig. 1.

the receiver noises, the output noise power is the sum of the two noise powers. However, the signal due to them is four times that for the case of one receiver. The output signal-to-noise ratio is therefore improved by a factor of 2.

The corresponding figures are

$$\sigma_{1d}^2 = \frac{\pi}{2} \sigma_n^2 \sqrt{\frac{\gamma}{\alpha}}$$

for modified square wave modulation and sine wave multiplier and

$$\sigma_{1d}^2 = \frac{4}{\pi} \sigma_n^2 \sqrt{\frac{\gamma}{\alpha}}$$

for modified square wave modulation and square wave multiplier. This last case is $\pi/2$ or 1.57 times as sensitive as the two receiver cross correlator.

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Application of Inductive Probability to Communications*

INDUCTIVE PROBABILITY

Although probability plays a key role in the study of radar and communication systems, engineers have, for the most part, concerned themselves with only one of its possible meanings. The consequence of this seems to be an unnecessarily restricted point of view which severely limits the usefulness of available information derived from observation. The concept of probability employed by engineers is the frequency concept of mathematical statistics: the relative frequency in the long run of one property of events or things with respect to another. Statements about frequency probability depend upon empirical procedure and the observation of facts.

Although many conceptions of probability are possible, Carnap¹ finds that these can essentially be reduced to two: the frequency concept, and the conception of probability as a certain logical relation between propositions. The latter concept has been termed logical or inductive probability, because its value is determined by logical analysis. This statement does not imply, however, that inductive probability has nothing to do with observational facts. On the contrary, inductive probability is relative to given evidence and has, in fact, two arguments, the hypothesis and the evidence, but since its statements are logically derived, each statement is logically true for each stage of the evidence. It may be interpreted as an estimate of relative frequency and as a fair betting quotient. If the relative frequency itself is known, then the relative frequency is the fair betting quotient.

From the point of view of radar and communications, the primary significance of inductive probability is that it avoids the pitfall of frequency probability which results from assigning *a priori* probabilities according to the principle of indifference, *i.e.*, assuming equal *a priori* probabilities in cases of complete ignorance. For example, there are eight possible three-digit, binary sequences, each of which is called a state description. The method of frequency probability is to assign a measure $M(S_i)$ to each state description S_i such that

$$\sum_i M(S_i) = 1$$

with each state description given a *a priori* equal measure. On the other hand, the eight possible three-digit, binary sequences can be considered in groups called structure descriptions such that the sequence consisting of three zeros is one structure description, the three sequences consisting of one unit digit and two zero digits a second, the three sequences consisting of two unit digits and one zero digit a third, and the sequence consisting of three unit digits a fourth. The method of inductive probability is to assign a measure $M(S_r)$ to each structure description such that

* Received by the IRE, June 23, 1958.

¹ D. G. Tucker, M. H. Graham, and S. J. Goldstein, Jr., "A comparison of two radiometer circuits," *Proc. IRE*, vol. 45, pp. 365-366; March, 1957.

² S. J. Goldstein, "A comparison of two radiometer circuits," *Proc. IRE*, vol. 43, pp. 1663-1666; November, 1955.

* Received by the IRE, June 26, 1958.

¹ R. Carnap, "Logical Foundations of Probability," University of Chicago Press, Chicago, Ill.; 1950.

$$\sum_r M(S_r) = 1$$

with each structure description given *a priori* equal measure. Moreover, if the inductive probability of a structure description is p and there are m members of this description, the inductive probability of each member is p/m .

The measure function $M(S_r)$ permits account to be taken of intuitive notions about learning by experience. Thus, if x_1, x_2, x_3 represent a sequence of binary digits, then $P(Ux_3/Ux_2 \text{ and } Ux_1) > P(Ux_3/Ux_1) > P(Ux_1)$ states that the probability of the third digit x_3 being a units' digit U , given that x_2 and x_1 are units' digits is greater than the probability of x_2 being a units' digit, given that x_1 is a units' digit, is greater than the probability of x_1 being a units' digit. Such a statement expresses the notion of the confirmation of a hypothesis by accumulating evidence.

The quantitative statement of inductive probability is given by the degree of confirmation $c^*(h, e_{-j})$ whose values are real numbers belonging to the interval 0-1. With reference to communications $c^*(h, e_{-j})$ may be read as the degree of confirmation, based on the available evidence e , for the hypothesis h that the next observation j will be a signal. It is given by the relation

$$c^*(h, e_{-j}) = \frac{s_2 + w_2}{s_1 + w_1 + s_2 + w_2} \quad (1)$$

where s_1 is the number of times the negative attribute is observed, w_1 is the logical width (that is, number of forms of this attribute), s_2 the number of times the positive attribute is observed, and w_2 the logical width of the positive attribute. In the example of the binary sequences a units digit might be called the positive attribute and the zero digit the negative attribute. The attribute appellations could, of course, be reversed if this is desired.

APPLICATION OF INDUCTIVE PROBABILITY

Errors in decision caused by use of a finite number of thresholds (usually one) and inappropriate settings of these thresholds limit detection probability, and these factors, plus, under certain conditions, an excessive number of integrations, limit information rate. Currently employed decision methods use constant threshold settings, independent of changing posterior probabilities. Inductive probability affords a means of altering threshold settings, and the consequences to probability of error and information rate will be examined.

In the discussion to follow, it will be assumed that the noise statistics are stationary, and that the signal statistics may vary with time.

A bidirectional, dual threshold communication system has been described elsewhere² with a capability for a significant reduction in probability of error, provided the thresholds can be set appropriately. A null zone is created between the two thresholds such that if the peak of a received waveform is within the null zone, the receiver requests

the transmitter over a feedback path to repeat the message. If the received waveform is above the upper threshold a positive signal is recorded, if below the lower threshold, a negative signal. In this system there are, therefore, three attributes: the positive signal attribute, the negative signal attribute, and the null or neutral attribute, only the first two of which are recorded. The probability of error of this system can be controlled by the threshold settings. Thus, if the thresholds are widely separated the probability of error is low, but the average number of transmissions per message symbol is high. On the other hand, if the thresholds are brought close together, the probability of error is relatively high but the average transmission time is low. It is found that performance can be considerably improved by integrating successive observations before making a decision, and when integration is combined with decision feedback, the method of operation is called cumulative decision feedback. In any case, the objective is to find that condition of operation which results in maximum information rate. This is, therefore, a problem in the setting of thresholds.

The difficulty with this system is that for a given noise power, but unknown signal amplitude, the appropriate threshold settings are unknown. Hence, a way must be found to estimate what these settings should be. It is suggested that inductive probability can be used to accomplish this result, and for clarification the distinction is drawn between the method of operation just described and the proposed modifications to it. In each case a decision is made about each message symbol as it comes along, but in the first method this is done by making a decision any time the peak of the received waveform is outside the threshold limits, whereas in the new method the decision for or against a positive attribute message symbol is made only after the number of repetitions of the message is sufficient to attain the specified degree of confirmation, with neutral attribute observations unrecorded. Moreover, in the new system the rate of increase in the degree of confirmation may be used to control the separation of the thresholds, that separation being sought which results in the maximum rate of increase. This rate, it will be noted, is controlled by the number of null observations or the one hand and by the concentration in favor of one kind of signal attribute over the other on the other hand, since if the numbers of observations of each kind of attribute remain more or less balanced, the degree of confirmation will remain in the neighborhood of 0.5. In comparing the performance of these two methods, it is noted that the first method arrives at decisions more rapidly than the new method but with threshold settings which may be inappropriate. This may not be serious for large signal-to-noise ratios and, in fact, for these the inductive probability method appears to be inefficient, because it calls for repetitions when they may be unnecessary, but for small signal-to-noise ratios, inappropriate threshold settings must result in poor decisions, although made with relative rapidity.

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A Transistor-Magnetic Core Binary Counter*

A technique for using transistor-magnetic core combinations to perform digital operations has been described by Guterman and Carey.¹ It is the purpose of this letter to describe an even simpler transistor-magnetic core binary counter that is also useful at counting rates as high as 2×10^6 pulses per second.

The counter consists of transistors and cores connected in such a manner that the count is indicated in binary form by the positive and negative residual magnetizations of the cores. The transistors are used as regenerative amplifiers to change the magnetic state of the cores when an input pulse is applied to the counter.

A single stage of the counter consists of a permalloy core having a rectangular hysteresis loop, a transistor, a silicon diode, and a resistor, all arranged as shown in Fig. 1(a).

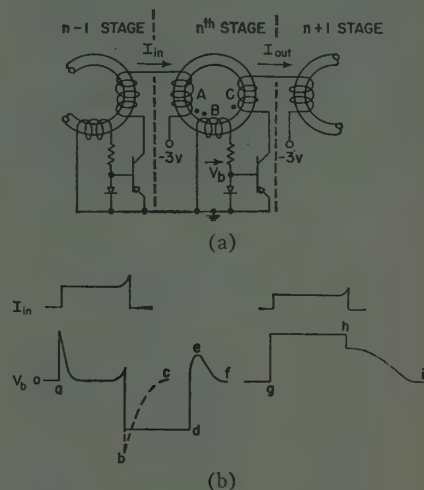


Fig. 1—(a) Circuit of binary counter. (b) Input current and base voltage waveforms.

Each stage of the counter is essentially a blocking oscillator that is triggered by alternate current pulses from the previous stage. For example, an output current pulse from stage $n-1$ [Fig. 1(a)] will trigger stage n if the core n is in the $+B_r$ state, but will not trigger this stage if the core is in the $-B_r$ state. In detail, if core n is in the $+B_r$ state, the current pulse from the previous stage will cause the core flux to change over the path $+B_r$ to $+B_m$ to $+B_r$ (Fig. 2) and produce the voltage a-b-c of Fig. 1(b). The negative voltage at point b is sufficient to trigger the transistor in stage n . The regenerative action of the transistor and core produces the waveform b-d-e-f as the flux in the core changes from $+B_r$ to $-B_m$ to $-B_r$. The next current pulse from stage $n-1$ will change the state of the core from $-B_r$ to $+B_m$ and in so doing will produce a positive voltage in winding B of sufficient duration to produce a large minority carrier storage in the diode. This carrier storage persists long enough to prevent the negative voltage

* Received by the IRE, July 21, 1958.

¹ S. S. Guterman and W. M. Carey, Jr., "A transistor-magnetic core circuit: a new device applied to digital computing techniques," 1955 IRE CONVENTION RECORD, pt. 4, pp. 84-94.

² B. Harris, A. Hauptschein, and L. S. Schwartz, "Optimum decision feedback systems," 1957 IRE NATIONAL CONVENTION RECORD, pt. 2, pp. 3-10.

in winding B (due to the turnoff of the current pulse from the previous stage) from triggering the transistor [see g-h-i of Fig. 1(b)]. The alternate outputs of stage n will trigger the $n+1$ stage in a similar manner.

The duration of the input current pulse to the n th stage can be adjusted so that it is just long enough to saturate the n th core by selecting the proper number of turns for the output winding of the core $n-1$.

An input current pulse of the proper length to operate the first stage of the counter could be obtained from a conventional blocking oscillator. However, the circuit shown in Fig. 3 has two advantages that make it superior to the blocking oscillator, namely, the circuit performs as a binary counter stage, and the duration of the output pulse is controlled by the saturation flux density of the core rather than the transistor parameters. To explain the operation of the circuit, assume that the core is in the $-B_r$ state and that the current I_1 due to the input pulse is in such a direction as to change the core in the direction of $+B_m$ (Fig. 2). The regenerative action of the transistor and core will cause I_1 to continue to flow until the core is saturated at $+B_m$. The base current of T_1 flowing through D_2 will produce sufficient hole storage in D_2 to prevent the triggering of T_2 by the regenerative turnoff of I_1 , thus leaving the core in the $+B_r$ state.

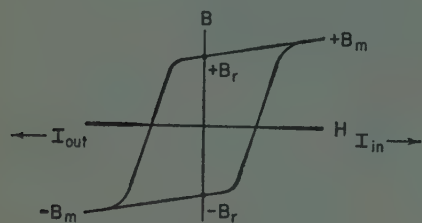


Fig. 2—Hysteresis loop of core.

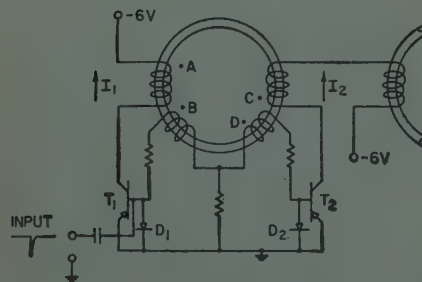


Fig. 3—Input stage for counter.

The current I_1 due to the next input signal will cause the flux to change from $+B_r$ to $+B_m$ in such a short time (approximately $0.1 \mu\text{sec}$) that no appreciable hole storage will be developed in D_2 . When I_1 turns off, T_2 will be triggered and change the flux in the core from $+B_r$ to $-B_m$. The hole storage in D_1 will prevent the triggering of T_1 by the turnoff of I_2 .

If winding c of Fig. 3 is connected directly to the -6 volt supply rather than to the next core, a simple complementing flip-flop circuit is obtained which can be used in an accumulator-type adder circuit and other digital applications.

The circuits described are capable of high counting rates and yet require very little power at low counting rates. For example, a five stage binary counter has a total power consumption of $40 \mu\text{W}$ when operated at a counting rate of 100 pulses per second. Counting rates as high as 2×10^6 per second have been obtained with commercially available cores. Good reliability is indicated by the fact that the circuit of Fig. 1 has been successfully operated over a temperature range of -65°F to $+160^\circ\text{F}$ with a supply voltage of -2.0 to -4.5 volts.

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Tropospheric Effects on 6-MC Pulses*

A test was performed at Boulder, Colo., during February, 1958, to make an independent measurement of the virtual height of echoes from a Model C-4 ionosphere recorder. The transmitted pulses from the recorder, of $50\text{-}\mu\text{sec}$ length, were observed at a temporary field site 5.2 km away, using loran equipment. The path ran in a north-south direction along the western edge of a flat plain about one mile above sea level. The land to the west of the path rises to peaks two or three thousand feet higher, and is mountainous with increasing elevation up to the Continental Divide, which has peaks twelve to fourteen thousand feet above sea level at a distance of 20 miles farther west.

In performing the test, the relative delays of the ground pulse and an ionospherically-reflected pulse were compared. For the best comparison, it was desired to adjust conditions so that the two received pulses would be of about the same height on an A-scan presentation and, of course, below receiver saturation.

The plane of the vertical delta transmitting antenna at the C-4 site was oriented normal to the direct path, as was the horizontal dipole at the receiving site. With these antennas and with the ionospheric conditions which prevailed at the time of the test, ground wave and sky wave received pulses were about equal in amplitude near 9 mc. The ground wave pulse was steady and the sky wave slowly fading.

It was desired to obtain another set of observations at 6 mc. At this frequency, and with the antennas as above, the ground pulse was steady but much larger than the sky pulse.

In order to obtain equal ground and sky wave pulse height at 6 mc, a vertical loop antenna was substituted for the dipole and rotated to reduce the ground wave pickup. When the plane of the loop was oriented to a direction almost at right angles to the path for a null in output, the ground wave amplitude suddenly dropped to where it was

comparable to that of the sky wave, but at this point it became much more unstable than the sky wave, being characterized by sharp minima within the width of the pulse, which rippled and fluctuated at a rate of several times per second.

When the direct ground wave from the transmitting antenna is discriminated against by the loop antenna, the chief remaining ground wave signal is believed to be of a multipath nature having been scattered from numerous off-path scatterers. The vast mountainous area to the west is considered to be the most probable source of such scatter, with fluctuations producing variable multipath phase interference, which distorts the pulse in the described manner.

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A New Type of Fading Observable on High-Frequency Radio Transmissions Propagated over Paths Crossing the Magnetic Equator*

During the course of a systematic study of the amplitude variations of the carrier-wave component of short-wave broadcasts propagated over long paths of varying orientations,¹ a type of fading has been identified which to the best of the authors' knowledge has not previously been described in the literature. Although existing data are fragmentary, the effect appears to be worth reporting at the present time in view of its evident importance in the design of high-frequency communications circuits crossing the magnetic equator.

Owing to multipath propagation, an HF carrier wave propagated over long distances via the ionosphere may be expected to fade in such a manner that its amplitude probability distribution is Rayleigh. The received energy is spread out into a spectrum, whose distribution of intensity per unit bandwidth vs frequency is roughly Gaussian. This is known to be generally true for a wide variety of path lengths and orientations.²

It is accordingly quite unexpected to encounter a situation in which the received carrier energy appears to be split into two independently fading components of comparable strength, separated in the frequency spectrum by several tens of cycles. The weaker of the two components beats with the stronger, closely resembling a modulation of the latter. Moreover, only two major components are found, and the fre-

* Received by the IRE, July 16, 1958. This work was supported by the AF Cambridge Res. Center, under contract AF-19-604-1830.

¹ K. C. Yeh and O. G. Villard, Jr., "On the fading and attenuation of high-frequency radio waves over a long path crossing the auroral zone," presented at URSI meeting, Washington, D. C.; April, 1958.

² G. L. Grisdale, J. G. Morris, and D. S. Palmer, "Fading of long-distance radio signals and a comparison of space- and polarization-diversity reception in the 6-18 mc/s range," *Proc. IEE*, vol. 104, pt. B, pp. 39-51; January, 1957.

* Received by the IRE, July 3, 1958.

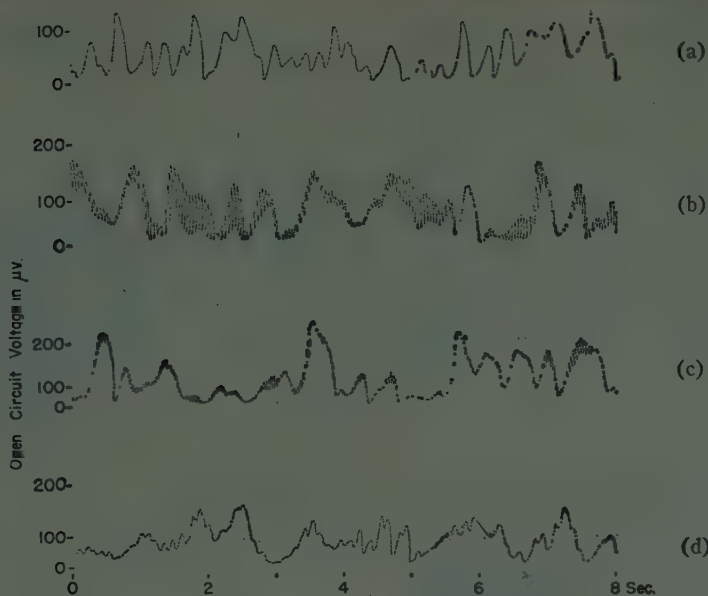


Fig. 1—Typical sequence showing the appearance and disappearance of Doppler fading on BBC's Singapore relay station on 9.690 mc, August 1, 1957. (a) 0250 PST. (b) 0300 PST. (c) 0320 PST. (d) 0335 PST.

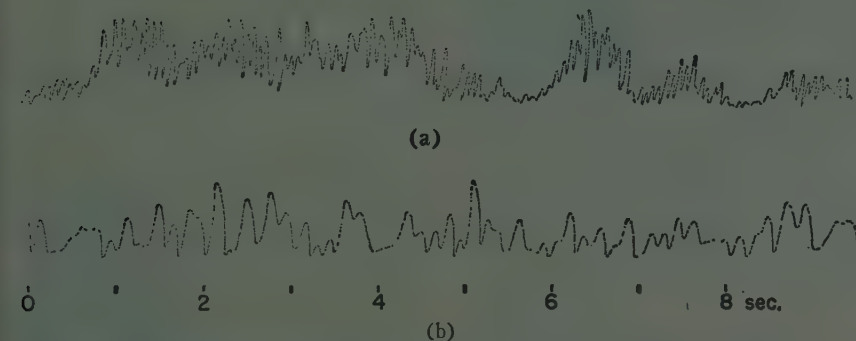


Fig. 2—Example of Doppler fading received simultaneously on two frequencies for BBC's Singapore relay station, 0735 PST, August 26, 1957. (a) 21.655 mc. (b) 9.690 mc.

frequency difference between them remains roughly constant for periods of the order of tens of minutes.

This effect has thus far been observed systematically only on signals which have crossed the magnetic equator. Fig. 1 shows a recording of the 9.690-mc transmission of the British Broadcasting Company's Far Eastern Relay Station, located at Singapore, Malaya. It was received at Palo Alto, Calif., via the short great-circle path, on a receiver having an intermediate-frequency bandwidth of the order of 200 cps. The frequency response of the ink recorder extends from zero to roughly 70 cps. This degree of selectivity has been found to be sufficient to reject virtually all program modulation except for infrequently-occurring deep bass notes which are readily recognizable as such.

The fading which is the subject of this communication will be observed as the relatively high-frequency fluctuation noticeable on the records for 0300 and 0320 PST in Fig. 1. It is probable that the effect is also present in the records for 0250 and 0335 PST, but at those times the "beating" frequency—if present—is so close to the individual-component fading frequency that a clear distinction cannot readily be made.

The "beating" frequency has these interesting properties: 1) When recordings can be made of signals from the same station at two radio frequencies simultaneously, the beat frequency is found to be very nearly proportional to the radio frequency. (See Fig. 2.) (During the five occasions on which this fading was observed simultaneously on 9.690 mc and 21.655 mc, the observed beat frequency ratio varied from 2.15 to 2.29 while the radio frequency ratio was 2.23. This circumstance would appear to rule out interference and spurious modulation as a source of the effect; in addition, it would appear that time delays associated with the approach to a critical frequency are also ruled out. 2) The beat frequency remains relatively constant for considerable periods of time, changing appreciably only in intervals of the order of fifteen minutes to half an hour. Because the first of these properties suggests that the fading may be due to the combination of a strongly Doppler-shifted carrier component with an unshifted one, the effect has been tentatively named "Doppler-fading."

The heavy lines in Fig. 3 show the times that this fading was looked for and found on the 9-mc Singapore transmissions during the month of August, 1957. (The light lines

indicate the times the effect was looked for but not found.) The transmissions were sampled during the periods shown, at irregular intervals 10 to 20 minutes apart. The station was on the air from 0100 to 0900 PST on 9 and 15 mc, and from 0500 to 0800 PST on 21 mc.

The higher frequencies were also sampled but since the effect was found most consistently on 9.6 mc, most of the observations were made on that frequency.

Rotatable Yagi antennas, roughly two-thirds of a wavelength high, were employed to record the 15 and 21-mc signal; at 9.6 mc a "maypole" arrangement of self-terminating sloping-Vee antennas was used. In all cases, the signal appeared to be coming from the short great-circle direction, as could readily be demonstrated by changing the beam directions.

Although the Doppler fading effect was seen during the month of August almost daily in the case of Singapore, it was found only sporadically in recordings made of Radio Australia (9 and 15 mc), Radio Peking (11 and 15 mc), and Station LRA in Buenos Aires (9 mc). It was not observed at all in a large number of recordings made of stations in England and Europe (9, 11, 15, and 21 mc).

A variation in the daily time of occurrence is suggested by the data of Fig. 3.

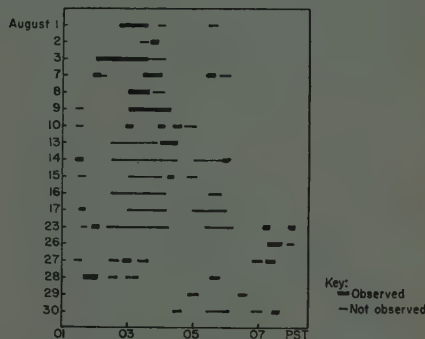


Fig. 3—Time of occurrence of Doppler fading for BBC's Singapore relay station on 9 mc in August, 1957.

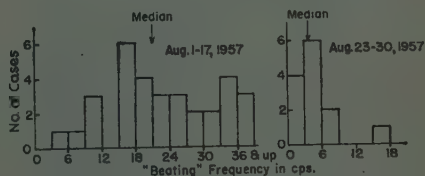


Fig. 4—To illustrate the change in "beating" frequency in August, 1957 for BBC's Singapore station on 9.690 mc.

Fig. 4 illustrates the change in median "beating" frequency which is observed if the data for August 1-17 are compared with those from August 23-30. Although the records taken on any given day are seldom continuous enough to permit a firm conclusion to be drawn, the Doppler beat is typically slow when it first appears, speeding up as time progresses, and slowing down again as the effect disappears. This trend is visible in Fig. 1.

An attempt to observe this fading during

one week of observations in January, 1958, yielded only one example.

No determination has been made of the direction of the presumed Doppler shift, and it is not known whether the beating effect is also observed on modulation side frequencies of the carrier wave. However it is a curious fact that presence or absence of the Doppler beating could not readily be determined by listening to the program modulation.

Although the data are too sparse as yet to permit firm conclusions to be drawn, it is tempting to ascribe this fading to a combination of conventional and tilt-supported propagation across the evening equatorial height bulge, as has been proposed by the late Sidney Stein.³ For example, at Singapore, Osborne⁴ reports that the minimum virtual height of the F layer may rise more than 100 km at a rate of 20 to 100 km/hr between 1700 and 2100 local time, depending on the season. One effect of such a marked increase in height—a phenomenon confined to equatorial latitudes—is to make possible tilt-supported ionospheric propagation of the type which involves two or more successive reflections from the F layer without intermediate reflection from the ground.⁵ Such tilt-supported propagation modes are often observed simultaneously with conventional multiple earth-ionosphere reflections. If both types of propagation have approximately equal strength, and the path of one varies in electrical length with respect to that of the other, interference effects can be expected which would be similar to those observed. (See Fig. 5.)

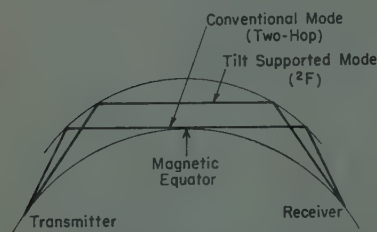


Fig. 5—To illustrate beating of two components of the same signal propagated via two differing modes. (Diagram not to scale.)

In view of the time of day at which the Doppler fading was observed (Singapore time is 9 hours earlier than Palo Alto time), and in view of the fact that paths crossing the magnetic equator are apparently favored, Stein's hypothesis is very tentatively offered in explanation of the present observations.

However, there is considerable difficulty in accounting for the high fading frequencies which have been observed, in view of their relatively long time duration. A relative path length change of roughly 2000 km/hr is required to account for a Doppler shift of 20 cps at a radio frequency of 9.7 mc; it is

not easy to imagine a means whereby such a path length change could be maintained for periods of the order of one hour.

It is possible that the present observations may in some way be related to the anomalous fading observed by Subba Rao and Somayajulu.⁶ However, their fading is about one order of magnitude slower, is relatively irregular, and is present all night long.

If the equatorial-bulge mode-interference hypothesis is correct, it might be possible to explain the absence of Doppler fading in the case of such stations as Radio Australia and LRA in Buenos Aires in terms of their relatively greater distance from the magnetic equator. (Their broadcasting schedules were relatively unfavorable, as well.) If reference is made to Fig. 11 of footnote 5, it can be seen that in order to excite both conventional and tilt-supported modes, it is desirable that the transmitted energy be incident on the ionospheric region containing the tilt over a wide range of angles of incidence. It is well known that signals which have traveled a long distance tend to have their energy restricted to a relatively narrow range of vertical angles. It is accordingly possible that in the case of stations far from the equator, the spread of vertical angles may not be sufficient to excite both types of modes at the tilted region.

Doppler fading of the sort described can have a major effect on the fading statistics of high-frequency signals propagated over transequatorial paths. Such rapid fading of the carrier in effect represents a spurious modulation which may become a matter for serious concern when data transmission systems utilizing the lower audio frequencies are employed.

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⁶ N. S. Subba Rao and V. V. Somayajulu, "A peculiar type of rapid fading in radio reception," *Nature*, vol. 163, p. 442; March, 1949.

A Note Concerning Instantaneous Frequency*

Recent discussions of instantaneous frequency have apparently not stressed the connection between the concept of instantaneous frequency and that of complex frequency as used in steady-state circuit analysis. It is the purpose of this note to point out how the definition of instantaneous frequency¹ follows from that of steady-state complex frequency in a straightforward fashion.

To establish the basis for subsequent generalization, the following facts of steady-state analysis are recalled:

* Received by the IRE, August 4, 1958.

¹ W. W. Harman, "Instantaneous frequency," *Proc. IRE*, vol. 42, p. 599; March, 1954.

1) The complex frequency of the function $f(t) = \exp(\sigma + i\omega)t$ is given by

$$\frac{d}{dt} [\log f(t)]. \quad (1)$$

2) Two complex conjugate frequencies are associated with the function $\sin \omega t$ (or $\cos \omega t$): the frequency with positive imaginary part is obtained by deleting the negative spectrum of the function and applying (1) to twice the remainder.

These notions may be extended to an arbitrary real function $f(t)$ with Fourier spectrum $F(\omega)$ by defining an associated complex function $f_+(t)$ as the inverse transform

$$F_+(\omega) = \begin{cases} 2F(\omega), & \omega > 0 \\ 0, & \omega < 0 \end{cases} \quad (2)$$

The complex instantaneous frequency $\Omega(t)$ of $f(t)$ is then found by applying (1):

$$\Omega(t) = \frac{d}{dt} [\log f_+(t)]. \quad (3)$$

One may write

$$F_+(\omega) = F(\omega) [1 + \operatorname{sgn} \omega]$$

and may thus identify

$$f_+(t) = [f(t) + if_H(t)], \quad (4)$$

where $f_H(t)$ is the Hilbert transform² of $f(t)$; i.e.,

$$f_H(t) = -\frac{1}{\pi} \int_{-\infty}^{+\infty} \frac{f(\tau) d\tau}{t - \tau}. \quad (5)$$

Then

$$\Omega(t) = \frac{d}{dt} \log [f^2(t) + f_H^2(t)]^{1/2} + i \frac{d}{dt} \tan^{-1} \frac{f_H(t)}{f(t)}, \quad (6)$$

and the imaginary part of this expression is the instantaneous frequency as defined by Harman.

With respect to the real part of (6), it may be of interest to consider the special case of an $f(t)$ whose spectrum is narrow as compared to its center frequency ω_0 . One may then identify the real part of (6) as the logarithmic derivative of the envelope

$$r(t) = [f^2(t) + f_H^2(t)]^{1/2}.$$

It is easily shown that the spectrum of $r^2(t)$ is given by

$$\mathcal{F}[r^2(t)] = \frac{1}{2\pi} \int_{-\infty}^{+\infty} F_+(x) F_+^*(x - \omega) dx.$$

The spectral extent of $r^2(t)$ is thus seen to be as narrow as is consistent with the spectral width of $f(t)$ about ω_0 , a property which one would intuitively demand of any reasonable definition of the envelope.

The author wishes to thank Drs. N. M. Abramson and W. W. Harman for their helpful comments.

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³ S. Stein, "The role of ionospheric-layer tilts in long-range high-frequency radio propagation," *J. Geophys. Res.*, vol. 63, pp. 217-241; March, 1958.

⁴ B. W. Osborne, "Ionospheric behaviour in the F_2 region at Singapore," *J. Atmos. Terr. Phys.*, vol. 2, pp. 66-78; July, 1951.

⁵ O. G. Villard, Jr., S. Stein, and K. C. Yeh, "Studies of transequatorial ionospheric propagation by the scatter-sounding method," *J. Geophys. Res.*, vol. 62, pp. 299-412; September, 1957.

² Multiplication of $F(\omega)$ by $\operatorname{sgn} \omega$ is equivalent to the convolution of $f(t)$ with $\mathcal{F}^{-1}[\operatorname{sgn} \omega] = -(i/\pi t)$ which leads to (5).

Contributors

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After two and one-half years of military service, he joined the staff of the Department of Electrical Engineering at Ohio State University, Columbus, Ohio, where he received the M.S. in electrical engineering in 1948 and the Ph.D. in 1951.

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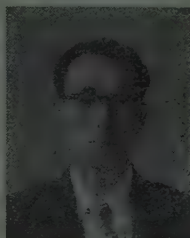
advanced Radio Technician School at Scott Field, Ill.

He has partially completed his undergraduate work toward the B.S. degree in electrical engineering at the University of Colorado, Boulder.

In 1955 he joined the National Bureau of Standards Central Radio Propagation Laboratory in Boulder, where he has been working on noise studies and radio system problems.



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From 1949 to 1957 he was engaged in research work on microwave spectroscopy, the atomic clock, and radio wave propagation at Kyoto University. Since 1957 he has continued his radio propagation work at Doshisha University.

He is a member of the Physical Society of Japan and the Institute of Electrical Communication Engineers of Japan.



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R. H. PANTELL

From 1954 to 1956 Dr. Pantell was assistant professor of electrical engineering at Stanford University and research associate in the Microwave Laboratory. He taught a graduate course in network synthesis, and did research on the development of a high-power traveling-wave tube. He was granted

a leave of absence from Stanford to become a visiting assistant professor at the University of Illinois during 1956-1957. There he worked on the generation of millimeter and submillimeter wavelengths, and taught courses in network synthesis and microwave measurements.

Dr. Pantell has resumed his position at Stanford and is continuing his research into the generation of microwave energy.

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Arthur D. Watt (SM'54) was born in Cedar Lake, Ind., on November 2, 1920. He received the B.S.E.E. degree from Purdue University, Lafayette, Ind., in 1942. From 1942 to 1951 he was employed at the Naval Research Laboratory, where he worked on transmitters, receivers, antennas, facsimile, television, communication theory, and communication system design problems. While at NRL, he took



A. D. WATT

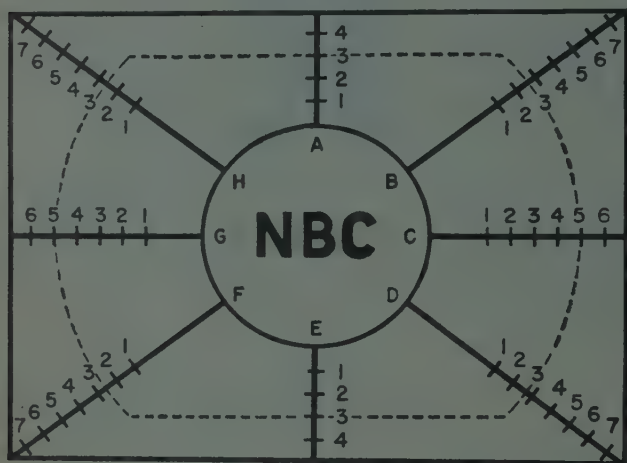
graduate work at the University of Maryland, College Park, Md.

In 1951 he joined the National Bureau of Standards Central Radio Propagation Laboratory in Boulder, Colo., where he has been concerned with modulation and radio system problems, including studies to optimize utilization of the frequency spectrum and signal to noise studies.

Mr. Watt is a member of HKN, a charter member of the Boulder RESA branch, and is active in URSI and CCIR work.

Scanning the TRANSACTIONS

Chopped off TV pictures are no novelty to viewers, broadcasters, or advertisers. The message that shows up on a home set with the telephone number across the bottom cut off has been an annoyance to people in the business ever since TV began broadcasting commercials. WRCA-TV in New York recently decided to do something about it. They broadcast a special pattern each morning for 15 minutes before regular air time and asked viewers to report how much of the pattern was visible on their sets. The pattern consisted of a number of radial lines marked off in segments equal to 5 per cent of the picture height, as shown below. As a result of this test, NBC was able to pin down the "safe area" of a TV picture, indicated by the dotted line. It should now be possible to insure that the top of an actor's head will be fully visible in the home. This will be a great boon to followers of Westerns, where the only way you can tell the hero from the villain is by his white hat. (C. L. Townsend, "TV receiver picture area losses," IRE TRANS. ON BROADCAST TRANSMISSION SYSTEMS, September, 1958.)



An automatic language translator that can translate scientific Russian into English is under development. The machine has a Russian-English "dictionary" capable of translating 160,000 Russian entries. The "dictionary" is on a glass disk, 10 inches in diameter, which rotates at 1200 rpm. The Russian words and their English meanings are photographically coded on the glass disk in black marks. Capacity of the disk is 60 million marks—6 million per square inch. Passage by an electronic "eye" translates the marks into electrical signals that are interpreted and translated by an electronic computer. The memory is capable of storing 30 million bits of digital information with a maximum access time to 50 milliseconds, and has a scanning rate of one million bits per second. (G. Shiner, "The USAF automatic language translator, Mark I," 1958 IRE NATIONAL CONVENTION RECORD, Part 4.)

Electronics is revolutionizing the highway building business. The usual method of selecting the best highway route calls for costly and time-consuming detailed surveys of each proposed route, followed by laborious hand plottings and calculations of elevations and the amount of digging and filling required along the entire route. During the last three to five years this time-honored method has been rapidly replaced by a new technique involving aerial photography, stereoscopy, and digital computers. Pairs of overlapping aerial photographs are first taken over the proposed route. The two photographs are then projected to form a three dimensional picture, and an observer manipulates an illuminated spot until it ap-

pears to him to rest on the ground. The position and a relative elevation of the spot are translated directly into digital data and fed to a computer which then quickly calculates from a series of such readings the highway profile and the amount of earth-moving work involved. Alternate routes can be explored in a matter of hours, instead of days or weeks. Most impressive of all, it is conservatively estimated that highway construction costs can be reduced by as much as 20 per cent, which in the next ten years might mean a saving of 20 billion dollars. (J. M. Cahn, "Automation in highway design," IRE TRANS. ON INDUSTRIAL ELECTRONICS, August, 1958.)

To aim a moon radar antenna, a punch card operated steering system has been developed that is twenty-five times more accurate than previous electronic systems. The system can be applied in modified form to tracking other celestial bodies, including satellites. Naval Observatory data regarding the orbit of the moon is punched into cards and fed to a digital computer, which then calculates where the moon will be at different instants with respect to the antenna. This information is stored on magnetic tapes and fed into an analog conversion system which provides a continuous flow of positional signals that keep the antenna aimed constantly and accurately at the moon as it moves across the sky.

Techniques for bouncing radar signals off the moon, pioneered by the Signal Corps in 1946, have recently taken on added importance in radio communications and radio astronomy. Last year the Naval Research Laboratory succeeded in receiving voice signals that were reflected by the moon, opening up the possibility of using the moon to relay long-distance radio transmissions. More recently, the same group used moon radar to measure the distance to the moon with an accuracy of within 1000 feet. (O. Guzmán, "Digital moon-radar antenna programmer with analog rate signal integrator," 1958 IRE NATIONAL CONVENTION RECORD, Part 4.)

A novel tube that tells time has been developed for measuring how long equipment or components have been operating. The tube consists of a small electrolytic cell containing a colored electrolyte, the color of which changes with the amount of dc current that has passed through it. At any time during the life of a particular piece of equipment, its "age" can be determined to within 5 per cent simply by unplugging the cell and measuring its color with a colorimeter. The device should prove particularly useful in obtaining reliability data, so that lifetimes of components and modules can be predicted and replacements made before a failure occurs. (W. Eriksen and E. Handley, "The tube that tells time," 1958 IRE NATIONAL CONVENTION RECORD, Part 3.)

Coded television pictures show promise of enabling bandwidth reductions of as much as 4 to 1. An experimental system has been developed which eliminates redundancies from the picture and takes advantage of certain properties of human vision to reduce the amount of information that has to be transmitted. A normal television camera output is fed into a small high-speed electronic computer which codes the video signal before transmission to the receiver, where a similar computer translates the code before presenting the picture on a normal television tube. An essential feature of the device is the temporary retention of the coded signal in electrostatic storage tubes to average out the information rate.

Existing methods for television transmission, such as microwave relay systems or coaxial cable, require the equivalent of 1000 telephone circuits for one video channel. As a result, such transmissions are very expensive. Furthermore, in the case of trans-Atlantic or trans-Pacific communication, television transmission is not possible at present because no

circuits of adequate bandwidth are available. Therefore, commercial long-distance relaying—especially transoceanic routes—will probably be the most important application of this new system. Military applications may also be important, since the “beyond the horizon” scatter propagation communication links now under construction will generally be able to handle the coded signal. Also, since the transmission is coded, it cannot be deciphered without special receiving equipment. If a moderate reduction in picture quality is acceptable, it is possible to construct an entirely transistorized version of very narrow bandwidth for field use. A similar system could also be used to transmit facsimile or news photos more rapidly than apparatus currently in use. (W. F. Schreiber and C. F. Knapp, “TV bandwidth reduction by digital coding,” 1958 IRE NATIONAL CONVENTION RECORD, Part 4.)

Radio engineers seem to be using telephones more and more for monitoring or controlling equipment in remote locations. The use of long distance telephone lines for gathering nuclear radiation data from unattended field stations was reported here only recently. Now a dialing circuit, costing all of \$150, has been proposed for the remote control of transmitting

equipment at an unattended antenna tower, so that such system parameters as frequency, polarization, and RF match can be independently adjusted over a single telephone line. (L. Young and G. M. Ward, “Telephone remote control circuit for an antenna site,” IRE TRANS. ON ANTENNAS AND PROPAGATION, October, 1958.)

Low-noise amplifiers are becoming of increasing interest as the number of available varieties of amplifying elements continues to grow. The circuit designer's problem is how to get the best noise performance from a composite amplifier in which individual units with specified noise properties are interconnected. General theorems on optimum possible performance were derived by H. A. Haus and R. B. Adler in *Proc. IRE*, August, 1958. As was promised there, the detailed proofs showing how these optimum results can actually be realized and the bases by which all amplifiers are classified and canonically represented have now been published in the appropriate *TRANSACTIONS*. (R. B. Adler and H. A. Haus, “Network realization of optimum amplifier noise performance” and “Canonical form of linear noisy networks,” IRE TRANS. ON CIRCUIT THEORY, September, 1958.)

Books

Feedback Theory and its Applications, by P. H. Hammond

Published (1958) by The Macmillan Co., 60 Fifth Ave., N. Y. 11, N. Y. 333 pages + 10 appendix pages + 4 index pages + xv pages. 204 figures. 8½ X 5½. \$7.00.

“The aim of this book,” according to the author, “is to present well-trying methods of linear and non-linear feedback system analysis and to illustrate their application to a variety of engineering devices which incorporate feedback in some form. The book is intended for graduate engineering and physics students and others who require an introduction to the subject and a view of its scope and future.”

In line with his stated purpose, the author—the principal scientific officer of the Royal Radar Establishment, Malvern, England—has produced a concise, clearly written, well-balanced text which covers the basic theory of linear and nonlinear feedback systems together with a number of applications. Of particular value are the well-chosen examples and the many interpretive comments of the author which reflect his extensive experience in this field, and which should go far in aiding the student to bridge the gap between the theory and the art of feedback system practice.

Feedback theory is introduced in chapter one by means of the differential equations of motion of a speed governor. A linear approximation is arrived at for this system and proceeding via the Laplace transformation a flow diagram representation in operational form is developed. After a discussion of the properties of feedback in chapter two, the important question of stability is considered in chapter three. The Routh criterion is stated but the major emphasis is on the

Nyquist criterion which is derived from first principles, and its application is illustrated by several clever examples. In chapter four graphical methods of representing the frequency response function and their use in stability determinations are developed. Applications of these techniques to certain electronic circuits are then described in chapters five and six, with particular emphasis being paid to the “operational amplifier” and its use as an analog computer element. The design of stabilizing networks is illustrated by the use of phase-gain characteristics.

Servomechanisms and other control systems are introduced in chapter seven, using linear theory. Examples are taken from hydraulic and electrical servomechanism practice. In chapter eight stabilization techniques are discussed, with the aid of numerous examples. Linear theory is then shown to be inadequate to explain the behavior of certain systems, and the remaining five chapters are devoted to nonlinear techniques—in particular the phase plane and the describing function. These techniques are illustrated by a study of the behavior of a positional servomechanism with inherent nonlinearities such as motor torque limitations, backlash in the gears, and coulomb friction and stiction in the load. A separate chapter is devoted to the study of on-off controlled servomechanisms; the properties of on-off elements are discussed by means of the phase plane and the describing function, and the optimization of transient performance is considered.

In the final chapter the application of electronic analog computers to the study of control systems with nonlinear elements is discussed. A design technique is illustrated

by means of a marine autopilot, with a full description of the steps needed to simulate the system on the computer.

While the selection of material in any book is always open to question, it is the opinion of this reviewer that the omission of root locus techniques mars an otherwise excellent introductory book. However, in spite of this omission, the book provides an excellent introduction to practical feedback systems.

Although the book treats a specialized subject, it is written in a simple manner with only a moderate amount of mathematics. It should be particularly useful to those interested in learning something of both the theoretical and practical aspects of feedback systems.

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Space Charge Waves and Slow Electromagnetic Waves, by A. H. W. Beck

Published (1958) by Pergamon Press, Inc., 122 E. 55 St., N. Y. 22, N. Y. 321 pages + 3 index pages + 70 appendix pages + xi pages. Illus. 8½ X 5½. \$15.00.

Imagine yourself starting work in a field of practical importance, a difficult field, and one in which a great deal of work has been done, a lot of it rather involved mathematically. What would help you most?

The best thing, of course, would be a wise and patient friend—a man familiar with nearly all of the published literature, a man with a sound practical background to enable him to sort the trivial or wrong from the correct and the important, a man with limitless hours to explain matters to you.

Except for the limitless hours for personal explanation, Mr. Beck is just this man, and

his new book, which seems to me even more useful than his earlier book, "Thermionic Valves," is the best written substitute for personal counsel concerning the theory of operation of microwave tubes.

This book covers a tremendous range. It starts out by describing the klystron, the traveling-wave tube and other microwave devices, and explaining space charge waves and the source of microwave energy. It then goes on to Maxwell's equations, slow-wave structures, including filter structures and helices, space-charge-wave theory, the related matter of plasma oscillations, matching boundary conditions at the input, the operation of klystrons, traveling-wave tubes and other tubes in terms of space-charge-wave theory, and noise phenomena. It includes references to nonlinear theory. A number of appendixes cover matters not treated in the main body of the text, including focusing of electron beams and coupled-mode theory.

It is hard to imagine a matter of any real importance to microwave tubes which isn't brought to the reader's attention and, best of all, sensibly evaluated. Of course, in many instances, explanations of the detail that the reader may desire can't be included, but there are very complete references to published work. The degree of the author's familiarity with the field is such that he in some instances gives references to unpublished work which has come his way. This rectitude will reassure if it does not help the reader.

Of course, the author is neither omniscient, infallible, nor gifted with second sight, and neither am I. He may very well have made errors of which I am unaware. He misses Walker's theory of the backward-wave oscillator, which antedates that of Heffner, and Walker's work on the conditions for waves in multivelocity flow. I think there is a view about the linearization of kinetic power expressions which he might well have expressed, and that a few pointed remarks about an alleged dispersion relation for plasma oscillations might not have been amiss. And, he missed by just a hair being able to include the new and important work of Siegman, Watkins and Hsieh which shows that multivelocity streams are not so irretrievably noisy as I and others had thought.

In other words, Mr. Beck is a human, not a superhuman, friend to those who work with microwave tubes. I think, however, that he may remain their best friend for some time.

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English-Russian, Russian-English Electronics Dictionary, compiled by Department of the Army

Published (1958) by McGraw-Hill Book Co., Inc., 330 W. 42 St., N. Y. 36. N. Y. 943 pages. 6 1/2 x 9 1/2. \$8.00.

The excellent "Russian-English, English-Russian Electronics Dictionary" compiled by the Signal Corps in 1955 has now been republished by McGraw-Hill between hard covers, and thus made even more widely available than before.

The volume contains separate Russian-English and English-Russian sections listing

over 22,000 technical words and expressions often encountered in electronic and communication engineering. Heaviest emphasis is on telecommunication engineering—radio transmitters, antennas, receivers, and wire communication apparatus and procedures. In these fields coverage is authoritative and complete. In radar, electronic navigation aids, acoustics, automatic control, electron devices, and measurements the listings are not quite so detailed, but entirely adequate for all but the most recent or specialized terms.

No volume of this size could cover all the many byways of contemporary electronic engineering in complete detail. This shows up here as a weakness in subjects with jargon which is fairly new (e.g., digital computers, solid state components, and information theory) or of a theoretical rather than experimental nature (e.g., some of the fringe fields of applied mathematics or physics).

Still, the book gives as good over-all coverage of electronics as is to be found in any single volume. Its worth is testified to by the fact that it was reprinted several years ago in the Soviet Union and is widely used there in preference to the available Soviet electronics dictionaries.

This reviewer can recommend the book highly to anyone who ever has occasion to look at the increasingly important Soviet electronics literature. However, he would like to point out that the original paper-bound volume is still available from the Superintendent of Documents in Washington for \$3.50, less than half the price of the new hard-cover reprint.

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Magnetic Tape Recording, by H. G. M. Spratt

Published (1958) by The Macmillan Co., 60 Fifth Ave., N. Y. 11. N. Y. 288 pages+7 index pages+23 appendix pages. Illus. 8 1/2 x 5 1/2. \$8.50.

This book is an extremely well written story of magnetic tape recording. It is organized on a very broad basis. Indeed, it embraces on the one hand the "Ultimate Nature of Magnetism" and on the other, detailed designs and applications of complete magnetic tape recorders. One slight flaw, from an American point of view, is that the equipment shown is all British or European. The book is very well constructed with a fine use of English and an excellent format. The illustrations are carefully done and, so far as we could determine, practically error-free.

From a discussion of the principles of magnetism, electroacoustics, and magnetic recording, the book proceeds into a discussion of tape manufacture and test and then into discussions of actual recording machines and their applications.

It is difficult from an American point of view to determine for whom the book is intended. Certainly, it is not for the student, since there are no problems and no derivations given. It can hardly be for the designer, since there is no development of design principles. It does, however, give several final design equations without development and shows a number of existing circuits. This

leaves as its potential audience those who wish to have a general knowledge of the practices of tape recording, primarily in the reproduction of speech and music, without expecting a detailed description of the field. For instance, in the discussion of tape manufacture, the various processes are described, including a discussion of the necessity of air conditioning, but there is very little basic chemistry.

Our main criticism of the book is that it is descriptive of a broad field but has little depth in any area.

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Television Engineering, Vol. IV: General Circuit Techniques, by S. W. Amos and D. C. Birkinshaw

Published (1958) by Iliffe and Sons Ltd., Dorset House, Stamford St., London S.E. 1, England. 260 pages+1 bibliography page+2 index pages. Illus. 8 1/2 x 5 1/2. 35s.

This is the fourth and final volume in a series on "Television Engineering" written by members of the BBC Engineering Division. Volume I deals with basic principles of television, particularly optics and camera tubes. Volume II is concerned with video amplifiers, including a special section on camera-head amplifiers. Volume III is on circuits commonly used for generating special waveforms, and their use in television. The present volume treats a number of circuit techniques which are used extensively in television, but do not properly belong to the earlier volumes. The books were written primarily for instructing the BBC staff, but Volume IV is discussed below from the standpoint of its usefulness to American readers, in and out of television engineering.

Topics include counter circuits, frequency dividers, dc clamp and restorer circuits, gamma-control (nonlinear characteristic) amplifiers, delay lines, fixed and variable equalizers, shunt-regulated amplifiers and cathode followers, line and field output stages, and electrical characteristics of scanning coils.

The previous knowledge expected of the reader is best illustrated by quoting the first sentence: "In a twin-interlaced television system the various pulses required in the sync signals or for camera operation have frequencies equal to the field frequency, line frequency or twice line frequency." The pace thus set is maintained throughout; in other words, this book is not for the beginner, but for the person already familiar with all the jargon of television circuitry. The innocent will find no help. This seems unfortunate, for most of the topics dealt with also have wide applications in fields other than television, particularly in experimental nuclear physics. I think that the number of potential readers would have been doubled by the addition of a three-page glossary of television terms.

The mathematical demands made on the reader are much more modest; anyone to whom the equation $L(di/dt) = j\omega Li$ expresses an obvious truth will have no difficulty here. Complete derivations are given for most of

the design equations, following the admirable custom of placing derivations in short appendixes at the end of each chapter. Of course, the American reader will have to realize that pF is the British form of $\mu\mu f$.

American engineering writers would do well to study this book for its literary quality alone. Ideas are expressed with a clarity and brevity very rare on this side of the Atlantic. One has the feeling that every single sentence has been scrutinized many times, every unnecessary word removed, and every possible ambiguity of meaning corrected. Because of this, the amount of material covered is greater than most American writers would be able to squeeze into a volume twice the size.

Another outstanding characteristic of this book is the number of illustrations. The use of circuit diagrams and diagrams showing the waveforms at various points in the circuits can only be described as lavish, and this is no small part of the reason so much can be said in so little space. Although the

text proper occupies only 250 pages, it includes 175 diagrams and two pages of plates. This feature, plus the clean typography and excellent quality of paper, make the book very easy and pleasant to read.

Anyone concerned with the practical design, use, or servicing of circuits of the type mentioned above will find this book one of the most useful he can locate. That it is completely sound technically, authoritative, and up-to-date, of course goes without saying.

E. T. JAYNES
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RECENT BOOKS

Bussard, R. W., and DeLauer, R. D. *Nuclear Rocket Propulsion*. McGraw-Hill Book Co., Inc., 330 W. 42 St., N. Y. 36, N. Y. \$10.00.
Eckman, D. P. *Automatic Process Control*. John Wiley and Sons, Inc., 440 Fourth Ave., N. Y. 16, N. Y. \$9.00.

Electron Tube Materials Compilation of ASTM Standards. American Society for Testing Materials, 1916 Race St., Philadelphia 3, Pa. \$3.50.
Feldtkeller, Richard. *Theorie der Spulen und Übertrager*. S. Hirzel, Stuttgart N, Birkenwaldstrasse 185, Germany. DM 24.
Gottlieb, I. *Basic Pulses*. John F. Rider, Inc., 116 W. 14 St., N. Y. 11, N. Y. \$3.50.
Krugman, Leonard. *Fundamentals of Transistors. Second Edition*. John F. Rider, Inc. 116 W. 14 St., N. Y. 11, N. Y. \$3.50.
Moir, James. *High Quality Sound Reproduction*. The Macmillan Co., 60 Fifth Ave., N. Y. 11, N. Y. \$14.00.
Schure, A., Ed. *Gas Tubes*. John F. Rider, Inc., 116 W. 14 St., N. Y. 11, N. Y. \$1.50.
Shand, E. B. *Glass Engineering Handbook*. McGraw-Hill Book Co., Inc., 330 W. 42 St., N. Y. 36, N. Y. \$10.00.
Taylor, Angus E. *Introduction to Functional Analysis*. John Wiley and Sons, Inc., 440 Fourth Ave., N. Y. 16, N. Y. \$12.50.

Abstracts of IRE TRANSACTIONS

The following issues of TRANSACTIONS have recently been published, and are now available from the Institute of Radio Engineers, Inc., 1 East 79th Street, New York 21, N. Y. at the following prices. The contents of each issue and, where available, abstracts of technical papers are given below.

Sponsoring Group	Publication	Group Members	IRE Members	Non-Members*
Antennas and Propagation	Vol. AP-6, No. 4	\$1.50	\$2.25	\$4.50
Broadcast and Television Receivers	Vol. BTR-4, No. 4	2.50	3.75	7.50
Broadcast Transmission Systems	PGBTS-11	0.65	0.95	1.95
Circuit Theory	Vol. CT-5, No. 3	1.35	2.05	4.05
Electronic Computers	Vol. EC-7, No. 3	1.50	2.25	4.50
Industrial Electronics	PGIE-7	1.85	2.75	5.55
Reliability and Quality Control	PGRQC-14	1.40	2.10	4.20

* Libraries and colleges may purchase copies at IRE Member rates.

Antennas and Propagation
VOL. AP-6, No. 4, OCTOBER, 1958
Contributions—The Effect of Echo on the Operation of High-Frequency Communication Circuits—D. K. Bailey (p. 325)
Echo on high-frequency communication services is defined as the simultaneous reception of signals over both major and minor arcs of the great circle connecting a transmitter and

receiver. Two distinct kinds of echo are recognized according to the illumination conditions under which they occur. Echo of the first kind is observed when the great-circle path coincides with the twilight zone surrounding the earth, whereas echo of the second kind, which can occur only on fairly long communication paths, is most severe when the short path is most intensely illuminated. Little can be done to obviate echo of the first kind and it is not, like echo of the second kind, amenable to prediction

by available methods of calculating sky-wave field intensities. Radio traffic data are cited which corroborate calculations and show both that echo of the second kind is more severe at times of maximum solar activity, and is less severe on higher frequencies. Conclusions are drawn concerning mode of operation and choice of operating frequency to minimize echo interference.
Foreground Terrain Effects on Overland UHF Transmissions—L. G. Trolese and L. J. Anderson (p. 330)
This paper describes an experimental study of the influence of the shape of foreground terrain profiles near terminals of UHF links on the received field. A gently rounded shape of the foreground profile causes a marked diffraction pattern to be superimposed on the normal variation of field strength with height. The diffraction geometry shows similarity to knife-edge geometry and the rounded terrain feature appears to act geometrically as an equivalent knife edge. The amplitude of the spatial variations in signal are, however, much greater than knife-edge theory predicts. A sizeable foreground diffraction enhancement of received field can be realized by locating the antenna at the height of the first diffraction maximum. Changing refraction due to meteorological variations can change both the position in height and intensity of the diffraction pattern.
A Rapid Beam-Swinging Experiment in Transhorizon Propagation—Alan T. Waterman, Jr. (p. 338)
By using a broadside phased array for an antenna, a narrow beam can be swung rapidly and in quick succession through a limited sector by fast control of the phasing, rather than by movement of the entire antenna structure. This technique is used at the receiving end of a 101-mile beyond-the-horizon transmission path

in order to probe the portion of the troposphere through which the signal is propagated. At the frequency employed of 3.12 kmc, a 0.49-degree beam is swung in azimuth through a 4.2-degree sector each tenth of a second.

A variety of phenomena are observed with this technique which have not been directly apparent in slower beam-swinging experiments. The beam-broadening effect attributed to atmospheric scattering is not always evident on any one sector scan. However, the change from scan to scan is frequently rapid enough so that a time average would show the broadening. At times the scan-to-scan changes are systematic and show a continuity indicative of a motion of the scattering or reflecting regions; in some cases this motion is too rapid to be accounted for by transport of air, thus implying a wave motion rippling through the atmosphere. At other times the atmospheric structure is too fine to be resolved by the beamwidth employed, and the time variations are too rapid to reveal a continuity from one scan to the next.

Effect of Mountains with Smooth Crests on Wave Propagation—I. P. Shkarofsky, H. E. J. Neugebauer, and M. P. Bachynski (p. 341)

A new method of solving the problem of diffraction of EM waves by the smooth crest of a perfectly reflecting cylindrical mountain has been previously reported. This paper presents the results in a form more suitable for practical applications. The theory is extended, and good agreement with model experiments is obtained for scattering angles up to 5 degrees. The procedure for including the effects of reflections from the ground on either side of the mountain is also indicated. A few examples illustrate cases encountered in practice, and exhibit effects up to 8 db compared with knife-edge diffraction.

Pattern of an Antenna on a Curved Lossy Surface—J. R. Wait and A. M. Conda (p. 348)

Extensive numerical results are presented for the radiation fields of electric and magnetic type antennas mounted on smooth curved surfaces of finite conductivity. The model chosen is a circular cylinder whose surface impedance is specified. A residue series representation is employed for the portion of space deep in the shadow while a geometrical-optical representation is used in the "lit" region. In the penumbra, the fields are expressed in terms of the "Fock functions." The results are also applicable to other smoothly varying curved surfaces such as spheres, parabolic cylinders, and paraboloids. As an application, the E-plane patterns are computed for a small loop antenna on a spherical earth for both sea and land illustrating the so-called cut-back effect.

Nonresonant Slotted Arrays—Andre Dion (p. 360)

The distribution of slot conductance of non-resonant arrays is obtained by considering the array as a continuous line source. Distributions of conductance per unit length for three Taylor aperture distributions are thus obtained. However, the discreteness of the array is retained for a discussion of second-order beams and for the development of a method leading to their suppression. The performance of an experimental array is described.

Gains of Finite-Size Corner-Reflector Antennas—H. V. Cottony and A. C. Wilson (p. 366)

An experimental corner reflector was erected at the Table Mesa antenna range near Boulder. The aperture angle of this antenna was made adjustable to any value between 20 and 180 degrees. The widths and lengths of the reflecting surfaces were each adjustable from 0.4 to 5.0 wavelengths. Measurements of gain were made for numerous combinations of lengths and widths of reflecting surfaces. These measurements were made with a half-wave dipole in the first, second and third maximum positions. The aperture angle was adjusted to maxi-

mize the gain. The principal results are presented in the form of contours of constant gain plotted for a range of widths and lengths of reflecting surfaces from 0.4 to 5.0 wavelengths. These graphs should be useful to a designer of corner-reflector antennas.

Scanning Surface Wave Antennas—Oblique Surface Waves Over a Corrugated Conductor—R. W. Hougardy and R. C. Hansen (p. 370)

The existence of a surface wave which propagates across a corrugated metallic surface at an oblique angle with the teeth is investigated both experimentally and theoretically in this paper. Expressions are derived which give the variation of the wave velocity and amplitude with the change of wave direction. Experimentally measured values of the surface velocity compare favorably with the theory.

The radiation pattern of an experimental antenna is given which demonstrates that a low sidelobe, narrow azimuth beam scannable to ± 30 degrees with a coscant-squared elevation pattern is attainable. A method of feeding this antenna to give a low silhouette, making the corrugated scanner antenna suitable for flush mounted applications, is illustrated.

Communications—Measurements of the Bandwidth of Radio Waves Propagated by the Troposphere Beyond the Horizon—J. H. Chisholm, L. P. Rainville, J. F. Roche, and H. G. Root (p. 377)

Remarks on the Fading of Scattered Radio Waves—Richard A. Silverman (p. 378)

Phantom Radar Targets at Millimeter Radio Wavelengths—C. W. Tolbert, A. W. Straiton, and C. O. Britt (p. 380)

This paper describes the techniques and the measured radar return from "phantom targets" using 8.6 and 4.3-millimeter radars. The radar returns are compared to the measured back-scattering cross section of water drops, insects, steam and other materials at 8.6-mm wavelength as measured by a CW radar at this wavelength.

Within the limits of the conditions used in the laboratory, it was impossible to produce returns from synthesized refractive index gradients of sufficient magnitude to account for those noted on the radar. It is concluded, therefore, that for the millimeter wavelengths and the short ranges considered, the observed phantom returns were due to solid or liquid particles in the atmosphere.

Telephone Remote Control Circuit for an Antenna Test Site—L. Young and G. M. Ward (p. 385)

A circuit is described which permits the remote control of several quantities, such as transmitter frequency, direction of polarization and RF match, at an unattended antenna tower. It requires only a single telephone line, which already exists for communication purposes at many test sites. Each quantity is controlled by a separate motor. The motors are controlled separately from the control end. This is achieved by adapting and installing a dialing circuit which allows, first, any desired motor to be "dialed"; next, to be controlled; and, finally, the line cleared so that another motor can be called.

The parts for the dialing circuit were purchased at a total cost of about \$150. Detailed circuit diagrams are given showing how the circuit is constructed.

Contributors (p. 387)

Annual Index 1958 (follows p. 388)

Broadcast and Television Receivers

VOL. BTR-4, No. 4,

SEPTEMBER, 1958

Faith of the Engineer (p. 1)

Professional Groups on Broadcast and Tele-

vision Receivers Administrative Committee (p. 2)

Vacuum-Tube Requirements in Vertical-Deflection Circuits—Karl W. Angel (p. 3)

This paper discusses linearity and efficiency problems which must be considered in the selection of an output tube for a vertical-deflection power amplifier. Because the purpose of the vertical-deflection power amplifier is to supply a given peak-to-peak current to the vertical yoke winding, the design problem is essentially one of matching the resistive component of the yoke to the tube characteristics in much the same manner as in audio-power amplifier design.

The Reaction of Sync Separators in Television Receivers to Impulse Noise—E. Luedicke (p. 15)

Transistor Thermal Stability—M. J. Hellstrom (p. 42)

The thermal stability of a transistor connected in a general bias circuit, with no signal applied, is analyzed. Graphical solutions are necessary to determine stability. Only cases in which the effects of temperature variations in input conductance are negligible will be considered.

Under certain conditions, frequently satisfied in practice, the solutions reduce to one which is more convenient to use. In a slightly smaller class of circuits still another simplification leads to a useful criterion which may be stated as follows.

Stability will exist when $SKEI_{c_0}/T_1 < 5.3$.

$S = dI_c/dI_{c_0}$, Stability Factor

K = Thermal Resistance, $^{\circ}\text{C}/\text{W}$

E = Average Collector to Base Voltage

I_{c_0}/T_1 = Leakage Current at a Temperature

$T_1 = T_a + KP_0$

T_a = Ambient Temperature

P_0 = Collector Dissipation in the Absence of any Leakage Current

In this case the equilibrium junction temperature T_j will not exceed T_1 by more than 14.4°C .

An illuminating interpretation of the stability factor, S , and a simple formula for calculating its value are incidental results of the analysis.

The Transistor and the Circuit Application Engineer—F. L. Abboud (p. 51)

To the engineer who has been working with vacuum tubes and vacuum-tube circuits, the transistor presents itself in many instances as a complicated electronic device. This paper presents the transistor to the engineer in the light of analogy and parallelism to the vacuum tube with which he is familiar, bearing in mind the inherent physical and operational differences between the transistor and the vacuum tube. Some of the problems met in transistor circuit design caused by the differences referred to above will be brought out where appropriate.

Transistor Circuitry Utilized in a New TV Sync Generator—L. M. Leeds (p. 60)

Receiver Video Transistor Amplifiers—R. G. Salaman (p. 68)

The problem of the common emitter video amplifier is divided into three categories according to the relative positions of device and load time constants. Optimum values of components are derived for each case. Two types of three transistor circuits are described; one of which uses a battery voltage of one half the peak to peak signal output voltage.

In general, this paper gives background to enable one to design a practical video amplifier for given output, gain and passband requirements.

Call for Papers for Spring Meeting (p. 77)

Improving the Television Horizontal Oscillator—Bill Feingold (p. 78)

Three popular methods of controlling the output amplitude of a stabilized multivibrator are discussed and their common problem of frequency variation with drive control indi-

cated. A corrected circuit is presented along with statistical data to substantiate the improvement.

Broadcast Transmission Systems

PGBTS-1, SEPTEMBER, 1958

TV Receiver Picture Area Losses—C. L. Townsend (p. 1)

The TV Helical Antenna Adapted to Structural Tower Shapes—R. E. Fisk (p. 4)

The side-fire helical antenna, successfully used for UHF and VHF high channel television transmission, has now been adapted for low channel VHF service. Investigation of properties of a helical radiator wound around a polygonal supporting structure has made possible the required increased bandwidth and provided directional patterns for special TV coverage applications. Through scale model work, a channel 2 directional antenna has been developed for installation around a triangular tower section.

An Audio Console Designed for the Future—A. C. Angus (p. 11)

Circuit Theory

VOL. CT-5, NO. 3, SEPTEMBER, 1958

Abstracts (p. 154)

Network Realization of Optimum Amplifier Noise Performance—R. B. Adler and H. A. Haus (p. 156)

Network realizations of the optimum noise performance (lowest noise figure at high gain) of a two-terminal-pair amplifier are presented. Two amplifier classes are distinguished: 1) networks that can both generate and absorb power and 2) networks that only generate power, or negative resistance networks. Amplifiers of class 1) can be optimized by first making them unilateral, subsequently employing input mismatch. Negative resistance amplifiers can be first brought into "canonic" form. Subsequent imbedding of part of the canonic network in an ideal circulator optimizes the noise performance. Both optimizations result in source impedances having a positive real part. High gain is achieved by subsequent cascading. The optimization using the ideal circulator yields masher noise performance optimization.

Canonical Form of Linear Noisy Networks—H. A. Haus and R. B. Adler (p. 161)

At any single frequency, every n -terminal-pair noisy linear network has at most n real parameters that are invariant with respect to all lossless "imbeddings" of that network. Such an "imbedding" is defined by constructing an arbitrary lossless $2n$ -terminal-pair network, n of whose terminal pairs are connected to those of the original network, and the remaining n of which form a new set of n terminal pairs. Moreover, by a suitable choice of this imbedding structure, the original network can always be reduced to a canonical form which places clearly in evidence its n invariants. The canonical form consists of n isolated one-terminal-pair networks each of which comprises a (negative or positive) resistance in series with a noise voltage generator, and these various noise generators are mutually uncorrelated. The n exchangeable powers from the n isolated terminal pairs are the n invariants of the original network.

The invariants have other physical meanings. Each meaning is best brought out by a corresponding particular matrix description of the network. Transformations between matrix descriptions are studied and applied to show that the invariants are interpretable as the n stationary values of the exchangeable power obtainable from any one of the new terminal pairs created by a lossless imbedding, as the

imbedding network is varied through all lossless forms.

Finally, the two invariants of a two-terminal-pair network are shown to fix the extrema of its noise measure, one of which is known to represent, for an amplifier, the minimum excess noise figure achievable at high gain.

Synthesis of Lossless Networks for Prescribed Transfer Impedances Between Several Current Sources and a Single Resistive Load—A. B. Macnee (p. 168)

A technique is presented for the synthesis of lossless networks open-circuited at one end and paralleled across a single resistance at the other end. The synthesis is for prescribed transfer impedances between the open-circuited terminals and the resistive termination. Such networks can be applied to a variety of frequency multiplexing problems, including the design of multichannel amplifiers. Examples are included, and some practical limitations of such networks are considered.

A Synthesis Procedure for Transmission Line Networks—Alfred I. Grayzel (p. 172)

Richards has shown that by a suitable frequency transformation, networks composed of transmission lines all of a fixed length and resistors behave over a range of frequencies zero to f_0 as lumped constant networks behave over the frequency range zero to infinity.

In the paper the synthesis procedure of a general class of lossless filters using transmission line components is considered. This is the class of filters having all of its transmission zeros at zero frequency and at infinite frequency in the transformed frequency plane, which corresponds to transmission zeros at zero frequency and frequency f_0 along the real frequency axis. This class includes the high-pass and low-pass configuration as special cases. It is proven that if a transmission characteristic is realizable using lumped constant elements, it can be realized in the transformed frequency plane using transmission line components. The transmission line components used are series or shunt shorted and open stubs and series lines. The series stubs are discussed and their feasibility demonstrated. It is shown that series transmission lines can be placed between elements whenever necessary, so that it is physically possible to build these networks.

Matrix Analysis of Oscillators and Transistor Applications—A. J. Cote, Jr. (p. 181)

The use of matrix techniques leads to the classification of feedback harmonic oscillators into four basic types. The oscillator is considered to be made up of two two-port networks: one contains the active element; the other the feedback network. The equations for oscillation are expressed in terms of the two-port parameters.

The method is applied specifically to the Hartley and Colpitts oscillators and their duals. The use of matrices in the analysis brings out the similarities between the oscillators. The Colpitts and Hartley circuits are of one class and require a small L/C ratio to reduce the effect of the active element upon frequencies, whereas their duals require a small C/L ratio.

While the equations are derived for the low frequency case, two methods of high-frequency analysis are presented.

The application of the equations to transistors is considered and several practical circuits for the dual oscillators are given. A short discussion of the bias elements and their effect on frequency and starting conditions is also included.

Axioms on Transactors—Gerald E. Sharpe (p. 189)

The introduction of semiconductor elements has greatly stimulated interest in active, lumped, nonbilateral network theory.

This paper sets out to answer the following fundamental question: Are there, by analogy to the three ideal passive elements, R , L and C ,

a group or set of ideal active elements, and if so, what are their properties?

The search for an answer leads to the postulate of an hypothesis on electromagnetism which states: Every electromagnetic action is of a causal and irreversible physical nature.

On this hypothesis is based a dual pair of ideal active elements also called the *transactor* elements. Their properties are discussed at length and a symbolism is introduced which extends and modifies network topology.

The study of the resistive feedback connection of these elements leads to the conclusion that Ohm's law in its present form is incompatible with a consistent, harmonious theory of networks. After lengthy discussion, Ohm's law is modified and an hypothesis on dissipation is stated.

Finally it is shown that only transactor elements having real transmittance need be considered fundamental and this is summarized by an hypothesis on activity.

On the Transient Responses of Ladder Networks—A. H. Zemanian and P. E. Fleischer (p. 197)

This paper considers bounds that may be obtained on the transient response of ladder networks. These results are developed by means of the superposition integral from the known bounds on the responses of the series and shunt elements of the ladder. Bounds on the response of a fairly general class of one-port networks are also given. Finally, several examples of the method are presented.

Theory of Low-Distortion Reproduction of FM Signals in Linear Systems—Elie J. Baghdady (p. 202)

Certain fundamental aspects of linear-system response to variable-frequency excitations are discussed. A unified argument is presented to simplify the derivation and define the convergence properties of the Carson and Fry and van der Pol-Stumpers expansions. Upper bounds on errors incurred in restricting each expansion to a finite number of terms are derived. This analysis leads to a more complete, more general statement of the conditions for low-distortion transmission and FM-to-AM conversion of FM signals than has heretofore been published. This statement shows that the most significant property of a frequency modulation is its maximum slope, and that the sluggishness properties of a linear system are completely specified by its "sluggishness ratio," $|Z''(j\omega)/Z(j\omega)|$, where $Z(j\omega)$ is the system function. Plots of this ratio for various important filters are presented. The newly derived condition for quasi-stationary response is proposed as a more complete criterion for specifying FM system bandwidths, and an analysis of the distortion in the quasi-stationary response is presented.

Minimum-Loss Two-Conductor Transmission Lines—Gordon Raisbeck (p. 214)

Of all two-conductor transmission lines in which the harmonic mean of the perimeters of the two conductors is fixed, the one having the lowest loss is a conventional round coaxial line. It is conjectured that the same is true of the class having fixed cross section area.

Realizability Conditions on n -Port Networks—Louis Weinberg and Paul Slepian (p. 217)

It is well known that the positive real (pr) concept is one of the most important in network theory. Its importance derives from the following two facts:

- 1) A necessary and sufficient condition for a real rational function to be realizable as the driving-point impedance of a one-port network is that it be a pr function.
- 2) A necessary and sufficient condition for a symmetric n th-order matrix of real rational functions to be realizable as the open-circuit impedance matrix of an n -port network is that it be a pr matrix.

Sets of necessary and sufficient conditions equivalent to the definition of a pr function and a pr matrix have been presented in the literature. In this paper new sets of necessary and sufficient conditions are formulated for a rational function and a matrix of rational functions to be pr. These conditions give insights that may be useful in research on unsolved synthesis problems; some of these problems are now being studied by the authors. When used for testing purposes none of the new conditions requires root solving, and thus in many cases much of the tedium of previous tests is eliminated.

Reviews of Current Literature (p. 222)

Correspondence (p. 224)

Electronic Computers

VOL. EC-7, No. 3, SEPTEMBER, 1958

The Chairman's Column—Willis H. Ware (p. 189)

Frontispiece—Willis H. Ware (p. 190)

Design of AC Computing Amplifiers Using Transistors—C. A. Krause and R. R. Lowe (p. 191)

A design philosophy for transistorized analog computing amplifiers is presented. A design procedure for a summing amplifier to drive a specific resolver in a 400-cps system is described, and the performance of the resulting circuit is evaluated. Whereas experience with vacuum tube amplifiers in similar applications has led to the conclusion that the amplifier input impedance should be as large as possible, the inverse is true in the transistor amplifier.

A Note on Contact Networks for Switching Functions of Four Variables—Roderick Gould (p. 196)

Several corrections are given to a recent tabulation of two-terminal contact networks realizing the switching functions of four variables. Nineteen new networks which are more economical in contacts than those previously tabulated are also presented and certain four-variable functions possessing a useful complementary relationship are listed. In conclusion this paper indicates an area where further work on four-variable contact network synthesis is needed.

On the Loop- and Node-Analysis Approaches to the Simulation of Electrical Networks—Joseph Otterman (p. 199)

The number of integrators in an analog-computer setup should be equal to the order of the differential equation describing the system. This paper presents a new procedure for tracing the loop currents which results in one-to-one correspondence between the number of integrators in the simulation setup and the count of independent energy-storing elements in the network, i.e., the degree of the system's characteristic equation. The generality of the procedure proves that it is always possible to trace the loop currents in such a way that excess integrators are avoided. The loop-analysis and the branch-variables-analysis approaches are discussed and examples given.

Generalized Parity Checking—Harvey L. Garner (p. 207)

The usual definition given for the parity check is unwieldy and not particularly suited for the analysis or the study of the arithmetic properties of parity checking. The definition of parity by means of congruences provides a convenient mathematical basis for the concepts of the parity check. In this paper congruence notation is used to generalize the concepts of parity to include nonbase two number systems. Consideration is given to the cases where the check base is equal to the number base, and where it is not equal to the number base. The arithmetic properties of each case are considered by means of congruences.

Investigations of Magnetic Amplifiers with Feedback—Harry J. Gray, Jr. (p. 213)

Sine wave carrier excited magnetic amplifiers have been investigated to determine if the figure of merit can be improved through the use of feedback techniques. It is shown that the power gain can be made unlimited but that a finite rise time is preserved. Hence the figure of merit as ordinarily defined becomes meaningless. It is shown, however, that voltage gain divided by rise time remains nearly constant under feedback and is a more suitably defined figure of merit.

A New Class of Digital Division Methods—James E. Robertson (p. 218)

This paper describes a class of division methods best suited for use in digital computers with facilities for floating point arithmetic. The division methods may be contrasted with conventional division procedures by considering the nature of each quotient digit as generated during the division process. In restoring division, each quotient digit has one of the values 0, 1, ..., $r-1$, for an arbitrary integer radix r . In nonrestoring division, each quotient digit has one of the values $-(r-1)$, ..., -1 , $+1$, ..., $+(r-1)$. For the division methods described here, each quotient digit has one of the values $-n$, $-(n-1)$, ..., $-1, 0, 1$, ..., $n-1$, n , where n is an integer such that $\frac{1}{2}(r-1) \leq n \leq r-1$. A method for serial conversion of the quotient digits to conventional (restoring) form is given. Examples of new division procedures for radix 4 and radix 10 are given.

Magnetic Core Pulse-Switching Circuits for Standard Packages—Jack L. Rosenfeld (p. 223)

A new method for the logical design of magnetic core pulse-switching circuits is presented. This method has features which make it excellent for use in standard packages. These features are the absence of spurious noise signals at the output; the fact that outputs are independent of the order of arrival of input pulses; the fact that interchanging components does not affect circuit behavior; and the fact that moderate changes in clock pulse amplitude and duration do not cause false operation. Furthermore, the number of components required by this system compares favorably with the numbers required by other systems. A computing system can be built by properly interconnecting a few different types of such packages.

The new system uses advance current drive but performs the logical operations with both forward and backward windings in an output network. The use of both types of windings permits a reduction in the total number of cores required.

Tests performed on actual circuits yielded very encouraging results. The circuits operated as predicted, and the performance was most satisfactory.

The Switching Characteristics of 4-79 Permalloy Cores with Different Anneals—T. D. Rossing, W. M. Overn, and V. J. Korkowski (p. 228)

The magnetic properties of 4-79 Permalloy cores, which have been annealed at different temperatures, are discussed. Cores annealed at relatively low temperatures are characterized by high coercivity, slower switching, insensitivity to strain, magnetization difficult to rotate, and insensitivity to an applied transverse field. Some cores exhibit a preference to one remanent state over the opposite state.

Formal Analysis and Synthesis of Bilateral Switching Networks—Raymond E. Miller (p. 231)

Formal procedures for the analysis and synthesis of two-terminal combinational bilateral switching networks are presented. A bilateral switching network is one which contains only elements having the same switching transmission characteristic in both directions.

Following the definitions for the terminol-

ogy and notation, where some new terms are introduced, the definitions for a series-parallel network, a bridge element, and a bridge network are given. A condition, called the bridge condition, to test a given transmission function for possible bridge network realizations is presented.

A stepwise decomposition procedure is developed which may be used for the analysis and synthesis of the series and parallel parts of the network. The steps are described both with linear graphs and connection matrices. The bridge condition partially formalizes bridge network synthesis. Redundant variables also are considered as an aid to network synthesis. Under certain conditions, the synthesis yields network realizations with the fewest possible number of elements.

A Transistor Pulse Generator for Digital Systems—Douglas J. Hamilton (p. 244)

A design procedure is developed for a new transistor pulse generator circuit suitable for use as a building block in a digital system. The circuit produces a pulse whose shape is relatively independent of variations in transistor parameters and load current. Pulse durations in the range 0.5 microsecond to 20 microseconds and load currents of several hundred milliamperes may be obtained.

Correction to "Logical Machine Design: A Selected Bibliography"—Douglas B. Netherwood (p. 250)

Correction to "Switching Functions of Three Variables"—D. W. Davies (p. 250)

Correspondence (p. 251)

Contributors (p. 252)

SENEWS, Science Education Subcommittee Newsletter (p. 254)

PGEC News (p. 259)

Industrial Electronics

PGIE-7, AUGUST, 1958

Automation in Highway Design—J. M. Cahn (p. 1)

The Semiautomatic Circuit Component Tester—F. C. Brammer (p. 4)

Process Instrumentation for the Measurement and Control of Level—G. Revesz (p. 11)

The use of capacitance-type measuring methods is described for indicating and controlling the level of liquid, granular or powdery materials. The purpose of this paper is twofold. First, it summarizes commercially available devices for various requirements (on-off control, proportional indication, proportional control, or combinations of these). Second, it formulates a method of analysis enabling users to choose suitable probe designs for specific applications.

Automatic Job Control Data System—C. Pilnick (p. 17)

In most industrial plants today, the system generally in use for acquiring and recording sufficient job data for accounting and planning purposes includes the following procedures:

- 1) Introduction of worker "time in, time out" and identification data onto a time card by means of a time clock.
- 2) Introduction of such variable data as job number, time spent on each job per day, craft code, etc., onto time sheets or records, usually performed manually.
- 3) Gathering of all such job data from various source records, again performed manually.
- 4) Transcribing the data into a format convenient for analysis and computation, either a manual or semiautomatic procedure.
- 5) Performing the desired computation or evaluation of the data for such end-item functions as payroll preparation, cost accounting, project analysis or compilation of statistics for job planning.

The complete job control data acquisition

and recording process involves laborious manual transcription with the possibility of human error at many stages. This field therefore represents an exceptionally fruitful one for the application of automatic techniques, if the cost of an automatic system is low enough to pay for itself in a reasonable period of time.

A basic automatic system is described below. The system is designed for maximum cost, but is sufficiently flexible so that modifications custom-tailored to almost any requirements may be incorporated.

Application of Automatic Techniques in the Handling of Physical Data for a Modern Refinery—W. G. Deutsch (p. 23)

The modern refinery is perhaps the test example of continuous flow processing in American industry. This paper shows how the concept of automatic data handling was applied in the design, construction, and instrumentation of one of the world's most modern refineries. Benefits made available through the integration of a modern automatic data handling system accrue not only from manpower savings, but from many other sources such as reduction in other instrument requirements, timeliness of information, etc.

The primary concern of this paper is to show how the automatic data handling system is incorporated in the conceptual design of the plant, and how once installed, it is commissioned, and its data correlated with that of other information sources in such a plant. As a further point of interest, other potential applications for automatic physical data handling systems are suggested by the author.

Automatic Techniques, Large Computers, and Engineering Calculations—V. Paschakis (p. 27)

This three-part paper first discusses (a) large-scale computers preparing automation; (b) computing devices in the automatized plant; (c) computing devices and engineering calculations. Next the author discusses the organization of a computing laboratory for engineering calculations. In the final part some implications of automation and large computing devices are considered.

Applying the Electro-Hydraulic Servo Valve to Industry—R. Spencer (p. 33)

The industrial control field is constantly adapting new techniques and procedures. These changes are motivated by industry's need to turn out their products faster and with greater precision. To make these improvements possible the manufacturers of mechanical, electrical, pneumatic, and hydraulic equipment are constantly developing new components and systems. Some components are developed on the basis of a general industry need and others for specific applications. The latter group of components, though designed for specific applications, become standard components as control-system designers begin to visualize how they may be applied to other control problems.

The electro-hydraulic servo valve is in its transition period. The success achieved in military and machine-tool applications indicates that its potential for industrial control problems is very high. To apply the servo valve, the industrial control-system designer must become familiar with its functions, capabilities, reliability, economics, and some special considerations. These factors are quite interrelated and it is the over-all evaluation of these factors which determines its suitability. This paper hopes to assist the industrial-control field toward a better understanding of the servo valve.

Basic Gages and Gaging Considerations for Automatic Machine Control—J. W. Hopper (p. 40)

In considering automatic techniques, many and varied definitions of greatly overused and misused words are applied. Certainly "automatic," "machine," and "control" are out in

front in so far as repetition is concerned. In order to chart a course through the material to be presented in this paper, I will arbitrarily consider that automatic machine control is a condition whereby material is manufactured by a piece of machinery, with suitable equipment to measure the product while it is being manufactured and provide corrections to the machine itself to produce material within desired limits. The gages in this configuration of measuring equipment will be dimensional measuring devices indicating diameter, length, thickness, and so on.

Logical Development of the Design for Sequential Control of Chemical Batch Processes—J. P. Laird (p. 44)

Chemical manufacturing processes frequently require safety interlock circuits which warn operating personnel of undesirable conditions or automatically act to avoid an accident. Batch-type manufacturing operations require that a succession of steps be carried out one after another, and successful operation depends on taking the proper action at the proper moment in a reproducible manner.

In the past there have been serious difficulties in communication among technical personnel who are concerned with these problems. Written descriptions are frequently either vague or confusing. What is needed are techniques which will aid in reading and writing of thought and reason. This paper attempts to aid in the solution of the problem.

A Survey of the Application of Automatic Devices for Electric Power Generation—A. C. Hartranft and F. H. Light (p. 55)

Twenty-five years ago power plant control and load dispatching were principally manual operations. Today, automatic devices are widely used and, in many cases, essential to safe and reliable operation. Much progress has been made in automation of power generation and distribution equipment. It is continuing. New developments include automatic data logging, automatic load control, network analysis by computers, and improved control systems.

It is the purpose of this survey to describe progress made in past years and briefly discuss new developments which are indicative of future trends. With this background, we are better able to judge the merits of automation and its potential advantages. These benefits are reduced operating costs, manpower savings, improved reliability, and more efficient use of manpower that has been relieved from routine duties.

The potential advantages of automation increase as electric systems grow in size and complexity. Large turbine-generating units require automatic controls and protective devices for reliable operation. Interconnection of systems makes automatic control necessary for regulation of interchange power flow.

An accurate evaluation of automatic control is difficult and requires careful study and judgment. Many of the advantages gained are intangible. Studies made by others provide valuable background information. This survey includes a bibliography of papers on automation in the electric power industry for the years 1950 to date.

The Application of the Punch Card to Automatic Weighing of Bulk Materials—W. M. Young (p. 63)

The automatic control of a dynamic batch-weighing system integrates many functions, more commonly associated with automation in the machine-tool industry. They are:

- 1) Power converting
- 2) Power actuating
- 3) Sensing
- 4) Regulating
- 5) Communicating
- 6) Programming
- 7) Computing
- 8) Data converting

9) Data storing

10) Data presenting.

Data storing and data presenting are the functions that directly involve the use of a punch card and similar information-storage media, and will be developed in detail.

Reliability and Quality Control

PGRQC-14, SEPTEMBER, 1958

The papers in this issue were presented at the Fourth National Symposium on Reliability and Quality Control, Washington, D. C., January 6 to 8, 1958. They were not available in time for printing in the *Proceedings* of that meeting.

The Impact of Reliability Requirements on Organization in the Manufacture of Airborne Electronic Equipment—J. J. Crowley (p. 1)

Current Military Reliability Specifications—E. F. Dertinger and D. W. Pertschuk (p. 6)

Reliability Techniques for Electronic Circuit Design—L. Hellerman and M. P. Racite (p. 9)

Air Force Electronic Reliability Program—J. S. Lambert (p. 17)

Reliable Design and Development Techniques—J. E. McGregor (p. 22)

Mechanical concepts must be applied to modify electronic circuit design in order that large scale computer equipment can attain practical levels of reliability. This paper cites some specific mechanical design problems with regard to the reliability of a particular computer system, the AN/FSQ-7.

The Navy Specification Program for Reliability—E. J. Nucci (p. 27)

The objective of this paper is to simply relate the role of the specification in the Navy's Electronics Reliability Program over the past years and to outline what appears to be the specification aspect of reliability for the future. In my discussion I will deal for the most part with full equipments and systems reliability and specifications.

Accelerated Life Test in Airframe Manufacture—N. H. Simpson (p. 33)

System Aspects—M. M. Tall (p. 50)

Reliable System Design by Part Engineering—C. G. Walance (p. 55)

This paper will concern itself with the organization and activity of a component application engineering organization and the part it plays in the development of electronic systems with particular emphasis on those aspects which influence the reliability of the system.

The Challenge of Reliability to Management—W. W. Wooldridge (p. 57)

Utilization of Component Part Reliability Information in Circuit Design—M. A. Xavier, L. L. Schneider, and P. Gottfried (p. 60)

Component part reliability testing programs of varying scope are in progress in many areas of the electronics industry today. These programs differ in magnitude, levels of environmental and electrical stress, and types of component parts tested, but properly designed programs have one aspect in common: They can result not only in reliability evaluation, but also in reliability improvement. This paper will discuss techniques for optimizing circuit reliability by application of component characteristic data obtained from reliability testing.

An Application of the Box Technique to the Evaluation of Electrical Components (Addendum)—R. Glaser (p. 69)

Presented here are examples of the statistical analysis of the responses for two of the variables, Pulse Response Factor, and Rcs referred to in the titled paper. It is intended to show a step-by-step procedure in analyzing the results with particular emphasis placed on the details in preparing the Analysis of Variance Table.

Abstracts and References

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NOTE: The Institute of Radio Engineers does not have available copies of the publications mentioned in these pages, nor does it have reprints of the articles abstracted. Correspondence regarding these articles and requests for their procurement should be addressed to the individual publications, not to the IRE.

Acoustics and Audio Frequencies.....	1980
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Circuits and Circuit Elements.....	1982
General Physics.....	1983
Geophysical and Extraterrestrial Phenomena.....	1984
Location and Aids to Navigation.....	1986
Materials and Subsidiary Techniques..	1987
Mathematics.....	1990
Measurements and Test Gear.....	1990
Other Applications of Radio and Electronics.....	1991
Propagation of Waves.....	1992
Reception.....	1992
Stations and Communication Systems..	1993
Subsidiary Apparatus.....	1993
Television and Phototelegraphy.....	1993
Transmission.....	1994
Tubes and Thermionics.....	1994
Miscellaneous.....	1994

The number in heavy type at the upper left of each Abstract is its Universal Decimal Classification number. The number in heavy type at the top right is the serial number of the Abstract. DC numbers marked with a dagger (†) must be regarded as provisional.

ACOUSTICS AND AUDIO FREQUENCIES

- 534:061.3** **3308**
Symposium on Unsolved Problems in Acoustics—(*J. Acoust. Soc. Amer.*, vol. 30, pp. 375–398; May, 1958.) The text is given of papers read at the 54th meeting of the Acoustical Society of America held at Michigan, October, 24–26, 1957, including the following:
1) Electroacoustics and Transducers—F. V. Hunt. (pp. 375–377.)
2) Speech and Communication—G. A. Miller. (pp. 397–398.)

- 534.1-8:538.222** **3309**
Paramagnetic Centres as Detectors of Ultrasonic Radiation at Microwave Frequencies—Kittel. (See 3416 below.)

- 534.13-8-16:538.69** **3310**
A Proposal for Determining the Fermi Surface by Magneto-acoustic Resonance—A. B. Pippard. (*Phil. Mag.*, vol. 2, pp. 1147–1148; September, 1957.)

- 534.22.08-16** **3311**
The Velocity of Sound in Metals at High Temperatures—J. F. W. Bell. (*Phil. Mag.*, vol. 2, pp. 1113–1120; September, 1957.) A pulse method of measuring the sound velocity in thin rods over a wide temperature range is described.

- 534.75** **3312**
Effect of the Transmission Characteristic of the Ear on the Threshold of Audibility—J. Zwislöcki. (*J. Acoust. Soc. Amer.*, vol. 30, pp. 430–432; May, 1958.) Sensitivity/frequency curves are given based on Békésy's results (e.g., 2121 of 1949).

The Index to the Abstracts and References published in the PROC. IRE from February, 1957 through January, 1958 is published by the PROC. IRE, May, 1958, Part II. It is also published by *Electronic and Radio Engineer*, incorporating *Wireless Engineer*, and included in the March, 1958 issue of that journal. Included with the Index is a selected list of journals scanned for abstracting with publishers' addresses.

- 534.75** **3313**
Creation of Pitch through Binaural Interaction—E. M. Cramer and W. H. Huggins. (*J. Acoust. Soc. Amer.*, vol. 30, pp. 413–417; May, 1958.) A faint pitch quality is detected when white noise presented at one ear is shifted in phase and presented to the other ear. An investigation of this phenomenon shows that phase information is of importance in pitch perception at frequencies up to 1.6 kc.

- 534.75:621.391** **3314**
Information Transmission with Elementary Auditory Displays—W. H. Sumby, D. Chambliss, and I. Pollack. (*J. Acoust. Soc. Amer.*, vol. 30, pp. 425–429; May, 1958.) The transmission of the letters of the alphabet by tone-coded signals is investigated using codes with two, three or five alternatives per letter and varying each of the four tonal variables. The highest reception rate was obtained with a three-alternative, frequency-coded display.

- 534.75:621.391** **3315**
Confidence Ratings and Message Reception for Filtered Speech—L. Decker and I. Pollack. (*J. Acoust. Soc. Amer.*, vol. 30, pp. 432–434; May, 1958.)

- 534.771:534.78** **3316**
Fundamentals of Testing the Hearing of Speech—F. J. Meister. (*Arch. Tech. Messen.*, no. 264, pp. 7–8; January, 1958.) The problems are outlined of selecting suitable speech material and of evaluating test results in physiological measurements of hearing ability. For details of normal measurement technique see *ibid.*, no. 265, pp. 21–24; February, 1958.

- 534.79** **3317**
Proposal for an Explanation of Limens of Loudness—J. R. Pierce. (*J. Acoust. Soc. Amer.*, vol. 30, pp. 418–420; May, 1958.) The root-mean-square deviation in the number of pulses produced in a given time is suggested as a measure of the limen of loudness.

ANTENNAS AND TRANSMISSION LINES

- 621.315.212.3** **3318**
Transmission Characteristics of a Three-Conductor Coaxial Transmission Line with Transpositions—G. Raisbeck and J. M. Manley. (*Bell Sys. Tech. J.*, vol. 37, pp. 835–876; July, 1958.) The design, manufacture and some experimental results are described. The effective cross-section of the center conductor is increased by using a solid central member and a thin concentric shell. The reduction of skin-effect losses, compared with a two conductor cable of the same diameter, gives lower

attenuation from 1 to 10 mc with a reduction of 17 per cent at 4 mc.

- 621.315.616** **3319**
Plastics in Cables—E. E. L. Winterborn. (*P.O. Elec. Eng. J.*, vol. 51, pp. 33–39; April, 1958.) The application to telephone exchanges, underground and antenna telephone cables, and to the protection of cables from corrosion, is discussed.

- 621.372** **3320**
Group and Phase Velocity—(*Wireless World*, vol. 64, pp. 445–449; September, 1958.) A simplified explanation of the terms is given and is applied to line and waveguide transmission.

- 621.372.2** **3321**
Calculation of Transmission Line Equations with New System Parameters—W. Doebke. (*Arch. elekt. Übertragung*, vol. 11, pp. 495–503; December, 1957.) Mathematical difficulties in the solution of line equations can be reduced by adopting the parameters on which the scattering-matrix concept is based. See e.g., 1660 of 1958 (Carlin).

- 621.372.2.029.6:621.317.74** **3322**
High-Frequency Measuring Lines—Moerder. (See 3577.)

- 621.372.22** **3323**
The Nonuniform Transmission Line as a Broadband Termination—I. Jacobs. (*Bell Sys. Tech. J.*, vol. 37, pp. 913–924; July, 1958.) The transmission-line equations are solved for a line in which the fractional change in shunt admittance/wavelength is constant. It is shown that a fixed length of line can be made to have as large an effective length as desired, and complete absorption of all energy will occur if the line has a small loss term.

- 621.372.8+621.396.677.7** **3324**
Some Aspects of Waveguide Technique—J. C. Parr. (*J. Telev. Soc.*, vol. 8, pp. 413–422; April/June, 1958.) Fundamental properties of electromagnetic waves and the generation of various modes of propagation inside a waveguide are discussed. Modes in resonant cavities are also considered, and three devices—the cavity wavemeter, the hybrid T junction and the slotted-waveguide array—are described.

- 621.372.8** **3325**
Determination of Higher-Order Propagating Modes in Waveguide Systems—M. P. Forrer and K. Tomiyasu. (*J. Appl. Phys.*, vol. 29, pp. 1040–1045; July, 1958.) A theoretical analysis and an experimental method are given

for determining the power level and relative phase of all propagating modes in a rectangular waveguide. Practical details are quoted for a 5 mw, S-band magnetron.

- 621.372.8 3326
Local Reflections in Waveguides of Variable Cross-Section—V. Pokrovskii, F. Ulinich, and S. Savvinykh. (*Dokl. Akad. Nauk S.S.S.R.*, vol. 120, pp. 504–506; May 21, 1958.) Mathematical analysis of the reflection and scattering produced by discontinuities.

- 621.372.823:621.317.7:538.566 3327
Double-Probe Polarimetric Analyser for the 1000-Mc/s Band—Picherit. (See 3574.)

- 621.372.823:621.372.83 3328
Circular-Waveguide Taper of Improved Design—H. G. Unger. (*Bell Sys. Tech. J.*, vol. 37, pp. 899–912; July, 1958.) Conical tapers with gradual change of cone angle transform cylindrical waves into spherical waves in the transition region. Optimal and almost optimal tapers are found for which the power conversion from TE₀₁ transmission to spurious modes is small for frequencies up to 75 kmc.

- 621.372.826:537.226 3329
Surface Waveguide—S. K. Chatterjee and R. Chatterjee. (*J. Inst. Telecommun. Eng., India*, vol. 4, pp. 90–95; March, 1958.) Characteristic equations are given for surface-wave propagation along a solid conductor embedded in three coaxial dielectrics. See also 1017 of 1958.

- 621.372.85:621.318.134 3330
Use of Microwave Ferrite Toroids to Eliminate External Magnets and Reduce Switching Power—M. A. Treuhaft and L. M. Silber. (*Proc. IRE.*, vol. 46, p. 1538; August, 1958.) Experiments show that toroids may replace slabs in some microwave devices, eliminating the need for external magnetizing currents and permitting higher switching rates.

- 621.372.852.22 3331
X-Band Phase Shifter without Moving Parts—W. H. Hewitt, Jr., and W. H. von Aulock. (*Electronics*, vol. 31, pp. 56–58; July 4, 1958.) The unit comprises two transversely magnetized ferrite slabs in the narrow walls of a rectangular waveguide. Continuous phase variation from 0 to 360 degrees is obtainable for up to 15 kw peak power. Maximum insertion loss is 0.75 db, and voltage SWR 1.08.

- 621.372.852.3:621.372.823 3332
The Frequency Response of Waveguide Potential Dividers with Coaxial Launching and Pick-Up—A. Sander. (*Nachrichtentech. Z.*, vol. 11, pp. 1–5; January, 1958.) The types of piston attenuator are discussed, with reference to theory presented earlier (2292 of 1956). Forty references.

- 621.372.852.323:621.318.134:621.317.74 3333
High-Power Testing of Ferrite Isolators—Wantuch. (See 3578.)

- 621.396.67:517.512.2(083.5) 3334
A New Table of the Amplitude Functions of the Iterated Sine and Cosine Integrals and Some Comments on the Aperiodic Functions in Hallén's Antenna Theory—P. O. Brundell. (*Acta polyt., Stockholm*, no. 217, 14 pp; 1957. *Kungl. tek. Högsk. Handl., Stockholm*, no. 108; 1957.) See also 1873 of 1955 (Hallén).

- 621.396.673.029.4 3335
A Study of Earth Currents near a VLF Monopole Antenna with a Radial Wire Ground System—J. R. Wait. (*Proc. IRE.*, vol. 46, pp. 1539–1541; August, 1958.) The results of experimental studies are briefly reported and

confirm the author's earlier theoretical work. See also 334 of 1955 (Wait and Pope).

- 621.396.677 3336
Suppression of Undesired Radiation of Directional HF Antennas and Associated Feed Lines—H. Brueckmann. (*Proc. IRE.*, vol. 46, pp. 1510–1516; August, 1958.) Practical measurements of rhombic antennas show large sidelobes which may contribute to interference in the HF band. Antenna arrays using nonuniform amplitude distributions and a tapered-aperture horn are briefly described, in which the sidelobes are substantially reduced. Coaxial feeders coupled to wide-band transformers are suggested in place of open-wire lines which are difficult to balance accurately.

- 621.396.677.001.57 3337
Use of Scale Model Techniques in the Design of V.H.F. and U.H.F. Antennas—F. J. H. Charman, J. Thraves and E. F. Walker. (*Electronic Eng.*, vol. 30, pp. 498–501; August, 1958.)

- 621.396.677.3:523.164 3338
Optimum Arrays for Direction Finding—N. F. Barber. (*N.Z. J. Sci.*, vol. 1, pp. 35–51; March, 1958.) The design of an array of receivers suitable for exploring the distribution of wave power with wave direction is discussed. Examples of practical arrays, including the Mills Cross, for the determination of power distribution with the minimum mean square error are examined.

- 621.396.677.3:523.164 3339
Gain Measurements of Large Antennas used in Interferometer and Cross-Type Radio Telescopes—A. G. Little. (*Aust. J. Phys.*, vol. 2, pp. 70–78; March, 1958.) A method is described using strong, discrete radio sources whose intensity need not be known. The method is applied to the 3.5-m Mills Cross radio telescope at Sydney [1126g of 1958 (Mills, et al.)].

- 621.396.677.73 3340
A New Ultra-Wide-Band Microwave Antenna—T. Sakurai. (*Rep. Elec. Commun. Lab., Japan*, vol. 6, pp. 40–45; February, 1958.) The antenna described is matched over the frequency band 4000–9400 mc with a voltage SWR better than 1.12. The gains are 32 and 40 db at the ends of the band.

- 621.396.677.8.029.6 3341
Polarization-Transforming Plane Reflector for Microwaves—J. Aagesen. (*Acta polyt., Stockholm*, no. 239, 27 pp.; 1957.) The infinite reflector investigated consists of a perfectly conducting surface in front of which is a parallel, anisotropically conducting surface. The intervening space is filled with a perfect dielectric. By a suitable choice of the thickness of the dielectric and the plane of polarization of the incident wave it is always possible to obtain a circularly polarized reflected wave.

- 621.396.677.833 3342
A 360° Scanning Microwave Reflection—J. A. C. Jackson and E. G. A. Goodall. (*Marconi Rev.*, vol. 21, no. 128, pp. 30–38; 1958.) The design and construction are described for a parabolic-torus reflector in the form of a radome with a wire grating inserted in its surface. A beam width of 3.5 degrees for –6 db with sidelobes at –25 db is possible for X-band frequencies using a 6-foot diameter reflector.

AUTOMATIC COMPUTERS

- 681.142 3343
Electronic Computer Research—(*Tech. News Bull., Natl. Bur. Stand.*, vol. 42, pp. 57–79; April, 1958.) A note on the research program of the National Bureau of Standards

followed by ten short papers with titles as under.

- A High-Speed Multiplier for Electronic Digital Computers—(pp. 58–59).
- Processing Pictorial Information on Digital Computers—(pp. 60–63).
- Low-Power Plug-In Packages for Electronic Computer Circuitry—(pp. 63–65).
- SEAC Converted to Applications Research Facility—(pp. 65–66).
- A Function Generator for Two Independent Variables—(p. 67).
- Man-Machine Simulation System—(pp. 68–70).
- Problem Solving on the High-Speed Computer—(pp. 71–75).
- Chemical Structure Searching with Automatic Computers—(pp. 75–76).
- Magnetic Amplifiers for Digital Computers—(pp. 77–78).
- Diode Amplifier Shift Register—(pp. 78–79).

- 681.142 3344
Electronic Computers 1957—K. Prause. (*VDI Z.*, vol. 100, pp. 701–708; June 1, 1958.) A survey with tabulated data on German equipment. Ninety-four references.

- 681.142 3345
Accuracy Control in Electronic Business Data Processing Systems—J. C. Hammerton. (*Electronic Eng.*, vol. 30, pp. 483–486; August, 1958.)

- 681.142 3346
Digital Codes in Data-Processing Systems—M. P. Atkinson. (*Trans. Soc. Instr. Tech.*, vol. 10, pp. 87–90; June, 1958.) Discussion on 1981 of 1958.

- 681.142 3347
Simple Digital Correlator—C. Collins. (*Rev. Sci. Instr.*, vol. 29, pp. 487–490; June, 1958.) "A description is given of a simple electronic correlator which employs punched-tape input and visual digital readout. Cold-cathode counting tubes are used in the arithmetic unit. Several basic design considerations are briefly discussed, and an outline is given of the recent application of the correlator to a problem in meteor physics."

- 681.142 3348
An Improved Technique for Fast Multiplication on Serial Digital Computers—M. Shimshoni. (*Electronic Eng.*, vol. 30, pp. 504–505; August, 1958.)

- 681.142 3349
Half-Adders Drives Simultaneous Computer—F. B. Maynard. (*Electronics*, vol. 31, pp. 80–82; July 18, 1958.) A combination of transistorized half and full adders, emitter followers, output amplifiers and multiplier gates provides simultaneous binary addition of digital inputs.

- 681.142 3350
Relay-Scanning-Design Technique Generates High Accuracy and Speed in Analogue-to-Digital Transducer Measurements—A. F. Kay. (*Commun. and Electronics*, no. 36, pp. 248–250; May, 1958.) The converter is designed to handle three decades of binary decimal pulses; each decimal unit is equivalent to 20 μ v input. The converter scans an internal voltage until it becomes equal to the unamplified input voltage and supplies a serial pulse output.

- 681.142 3351
The Design of Function Generators using Short-Time Memory Devices and Nonlinear Elements—A. W. Revay and D. J. Ford. (*Commun. and Electronics*, no. 36, pp. 143–152; May, 1958.) The various types of function

generator discussed have easily controllable output waveforms which can be made to approximate to any desired shape with a high degree of accuracy.

681.142 3352

An Electronic Differential Analyser—A. K. Choudhury and B. R. Nag. (*Indian J. Phys.*, vol. 32, pp. 91–108; February, 1958.) Equations are derived to show the effect of errors due to circuit elements, and some experimentally obtained solutions are compared with calculated values.

681.142:512.3 3353

On the Application of an Electronic Differential Analyser for Finding the Roots of a Polynomial—B. R. Nag. (*Indian J. Phys.*, vol. 32, pp. 212–217; May, 1958.) A transfer function is used with the polynomial as numerator and another suitable function as denominator. The roots are given by the zeros of the output of the system.

681.142:517.9 3354

Digital Field Computers—B. Meltzer and I. F. Brown. (*Nature, London*, vol. 181, pp. 1384–1385; May 17, 1958.) To eliminate the speed limitation of conventional digital techniques for field computations, a nonuniversal unitary system is proposed, based on the analogy between electron flow through a resistance network and the flow of pulses through a network of computer units. An integral number N is represented by N pulses, and a basic unit generates a train of $\frac{1}{2}(N_1 + N_2)$ synchronized pulses from two input pulse trains of N_1 and N_2 pulses. The interconnection of a lattice of basic units gives a finite-difference representation of the general field equation.

681.142:518.4 3355

An Automatic Graph Plotter—J. J. Morrison. (*Trans. Soc. Instr. Tech.*, vol. 10, pp. 55–66; June, 1958.) The adaptation of an analog plotting table for accepting input data in digital form is described.

681.142:621.039 3356

The Application of Digital Computers to Nuclear-Reactor Design—J. Howlett. (*Proc. IEE*, vol. 105, pp. 331–336; July, 1958. Discussion, pp. 365–369.) The main computational problems are reviewed, together with examples of the treatment of neutron transport problems. An assessment is made of the performance requirements of future computers.

681.142:621.372.5 3357

Use of Laguerre Filters for Realisation of Time Functions and Delay—A. K. Choudhury and N. B. Chakrabarti. (*Indian J. Phys.*, vol. 32, pp. 205–211; May, 1958.)

681.142:621.385.832 3358

Analogue Multiplier and Function Generator with Cathode-Ray Tube—A. K. Choudhury and B. R. Nag. (*Indian J. Phys.*, vol. 32, pp. 141–148; March, 1958.) A capacitive pick-up device is mounted outside the CR tube in front of the screen; it is easily replaced so that the same tube can be used as multiplier or for generating different types of functions.

681.142:621.396.11 3359

An Electronic Computer for Statistical Analysis of Radio Propagation Data—M. Grönlund and C. O. Lund. (*Acta polyt., Stockholm*, no. 222, 26 pp., 18 plates; 1957.)

CIRCUITS AND CIRCUIT ELEMENTS

621.3.049.75 3360

Printed Circuits—A. Roos. (*Metal Ind., Lond.*, vol. 92, pp. 467–470; June 6, 1958.) Review of materials and manufacturing processes.

621.318.4.045 3361

Coils for Magnetic Fields—G. M. Clarke. (*Electronic Radio Eng.*, vol. 35, pp. 298–306; August, 1958 and pp. 340–344; September, 1958.) A comparison between wire-wound, foil-wound and coaxial-cable-wound solenoids, considering the limitations of temperature-rise and weight. Equations relating field, power and internal temperature difference are obtained from which the performance of any coil can be calculated. The relative advantages of Al or Cu windings are considered.

621.319.4 3362

A Note on the Self-Resonance of Ceramic Capacitors—J. Bork. (*Proc. IRE, Aust.*, vol. 18, pp. 159–162; May, 1957.) Details of changes in self-resonant frequency with a capacitor type, length of connecting leads and method of mounting are given. Practical applications of the self-resonance of these components in VHF circuits are suggested.

621.372:512.831 3363

Certain Applications of Matrices to Circuit Theory—L. A. Pipes. (*Commun. and Electronics*, no. 36, pp. 251–256; May, 1958.) Matrices can be constructed for circuits so that their eigenvalues and vectors relate to the circuit parameters. Propagation constants, characteristic impedances and symmetrical components in polyphase systems are considered from this point of view.

621.372.2:621.318.5 3364

Synthesis of Series-Parallel Network Switching Functions—W. Semon. (*Bell Sys. Tech. J.*, vol. 37, pp. 877–898; July, 1958.) "From the switching functions of n variables, those which correspond to networks are abstracted and called network functions. Properties of those network functions corresponding to series-parallel networks are studied and a method for synthesis is developed."

621.372.414 3365

High-Power Radio-Frequency Broad-Band Transformers—E. R. Broad. (*P.O. Elec. Eng. J.*, vol. 51, pp. 8–13; April, 1958.) "The design of wide-band transformers composed of simple transmission line elements and capable of handling radio-frequency power of the order of 20 kw is discussed. Examples are given of devices matching 75-ohm coaxial cable to balanced-pair transmission lines with a standing-wave ratio of less than 1.3 over the band 4–28 mc."

621.372.51 3366

Complex Matching—D. Steffen. (*Elektronische Rundschau*, vol. 12, pp. 3–9; January, 1958.) The conditions are investigated for obtaining maximum real power at the input of a complex load matched to a generator with complex internal impedance.

621.372.54:621.396.96 3367

Analysis and Synthesis of Delay-Line Periodic Filters—H. Urkowitz. (*IRE TRANS. ON CIRCUIT THEORY*, vol. CT-4, pp. 41–53; June, 1957. Abstract, *PROC. IRE*, vol. 45, p. 1432; October, 1957.)

621.372.543.2 3368

Pulse Distortion by Band Filters—K. Emden. (*Arch. elekt. Übertragung*, vol. 11, pp. 509–512; December, 1957.) The roots of the homogeneous differential equations for image-parameter (Zobel) band-pass filters with one to four stages are tabulated. The integration constants are determined for the case of a square-wave-modulated carrier equal to the mid-band frequency of the filter.

621.372.543.2 3369

Design of Unsymmetrical Band-Pass Filters—R. F. Baum. (*IRE TRANS. ON CIRCUIT*

THEORY, vol. CT-4, pp. 33–40; June, 1957. Abstract, *PROC. IRE*, vol. 45, pp. 1431–1432; October, 1957.)

621.372.553 3370

Simplifying Phase Equalizer Design—W. J. Judge. (*Electronic Ind.*, vol. 17, pp. 76–77; April, 1958.) A graphical method using bridged-T and all-pass lattice networks.

621.372.57:621.314.7 3371

Power Amplification \times Bandwidth Figure of Merit for Transducers including Transistors—L. J. Giacoletto. (*J. Electronics Control*, vol. 4, pp. 515–522; June, 1958.) A figure of merit based on spot-frequency maximum power amplification \times bandwidth is derived for a transducer which is unilateralized and conjugately matched, the result being simplified by assuming a bell-shaped frequency response. Specific formulas are given for tube and transistor circuits. See e.g., 2238 of 1953.

621.372.6 3372

On the Synthesis of Three-Terminal Networks Composed of Two Kinds of Elements—K. M. Adams. (*Philips Res. Rep.*, vol. 13, pp. 201–264; June, 1958.) "A set of necessary and sufficient conditions and a method of realization of all sets of series-parallel LC three-terminal network functions from the zeroth to the sixth degree are given."

621.372.632:621.396.621 3373

A Low-Noise Crystal-Controlled Converter for 144 Mc/s—G. R. Jessop. (*R.S.G.B. Bull.*, vol. 33, pp. 510–512; May, 1958.) Construction details of a converter providing satisfactory reception of signals of about 3 db above noise level.

621.373.1.018.756 3374

Millimicrosecond Pulse Generator—O. H. Davie. (*Electronic Radio Eng.*, vol. 35, pp. 332–335; September, 1958.) The generator uses a length of high-frequency cable which is charged from a known dc potential. The cable is then discharged into the load by a magnetically operated mercury switch at pulse repetition frequencies up to 120 cps for pulses of 1- μ sec rise time.

621.373.1.029.4 3375

Calculations for a Capacitor with Rotating Armatures Piloting a Very-Low-Frequency Generator—P. Dupin, R. Lacoste, and H. Martinot. (*Compt. Rend. Acad. Sci., Paris*, vol. 246, pp. 1172–1175; February 24, 1958.) See 1699 of 1957 (Dupin).

621.373.421.13 3376

Fluctuations in Quartz Crystal Oscillators—M. E. Zhabotinskii and P. E. Zil'berman. (*Dokl. Akad. Nauk S.S.S.R.*, vol. 119, pp. 918–921; April 11, 1958.) Results of an analysis using symbolic differential equations show that the noise and thermal fluctuations are not determining factors for stability. See also 1996 of 1956 (Rytov).

621.373.421.13 3377

Thermally Compensated Crystal Oscillator—(*Wireless World*, vol. 64, p. 441; September, 1958.) Frequency stabilization without the use of a temperature-controlled oven is obtained by varying the effective shunt load of the crystal, a thermistor head being the temperature-sensitive element.

621.373.52.072.6 3378

Transistor Circuit Varies Reactance—F. F. Radcliffe. (*Electronics*, vol. 31, pp. 76–80; July 4, 1958.) Frequency control of a 2.5-kc oscillator to within 0.1 cps is achieved by means of a variable-reactance circuit which produces an effective capacitance change of up to 3500 pf for a change in emitter current from zero to 700 μ a.

621.374.3:681.142 3379

A Neon Pulsar for the Computer Laboratory—R. L. Ives. (*Electronic Ind.*, vol. 17, pp. 98–100; April, 1958.) An output of 70 volt peak, positive or negative, at pulse repetition frequencies from less than 1 cps to 2.5 kc is obtained.

621.374.32 3380

High-Speed Pulse Amplitude Discriminator—F. J. M. Farley. (*Rev. Sci. Instr.*, vol. 29, pp. 595–596; July, 1958.) A circuit is described for use in fast counting systems. It handles pulses of amplitude 1–21 volts generating a positive output pulse of constant amplitude whose length is determined by the length of the input pulse. Dead time is about 20 μ sec and peaks 40 μ sec apart are separated.

621.375.012:621.396.822 3381

Optimum Noise Performance of Linear Amplifiers—H. A. Haus and R. B. Adler. (*Proc. IRE*, vol. 46, pp. 1517–1533; August, 1958.) A single quantitative measure of amplifier "spot noise" performance $(M_e)_{opt}$ is established which removes difficulties associated with the effect of feedback on the noise figure as it is a function only of the amplifier noise and circuit parameters. It determines the lowest noise figure obtainable at high gain with a given amplifier used alone, or passively connected to other amplifiers of the same $(M_e)_{opt}$, and it provides an index of the absolute quality of noise performance.

621.375.024 3382

Performance Calculations for DC Chopper Amplifiers—I. C. Hutcheon. (*Electronic Eng.*, vol. 30, pp. 476–480; August, 1958.) Switched chopping and demodulating circuits are analyzed, and methods of calculating the essential parameters are described.

621.375.024:[621.317.725:621.385 3383

D.C. Amplifier Expands Input Voltage Range—V. D. Schurr. (*Electronics*, vol. 31, pp. 87–89; June 6, 1958.) A direct-coupled dc amplifier with infinite input-voltage range and infinite input impedance is described, and details are given of its application in a differential tube-voltmeter without input voltage dividers for measurements at mean levels between –150 and +300 volts.

621.375+621.385].029.65 3384

The Generation and Amplification of Millimetre Waves—W. Kleen and K. Pöschl. (*Nachricht. Z.*, vol. 11, pp. 8–19; January, 1958 and pp. 77–84; February, 1958.) A detailed survey of techniques and devices including the maser and the harmodotron. Eighty-eight references.

621.375.126:621.396.96 3385

The Design of Primary and Secondary Radar I.F. Amplifiers—N. N. Patla. (*J. Inst. Telecommun. Eng., India*, vol. 4, pp. 102–111; March, 1958.) The features of synchronous and stagger-tuned circuit arrangements are discussed and design procedures outlined. Practical considerations such as feedback coil design and heat dissipation, and the design of amplifiers having logarithmic characteristics are also covered.

621.375.2:621.317.755 3386

Direct or A.C. Coupling for Deflexion Amplifiers—H. L. Mansford. (*Electronic Eng.*, vol. 30, pp. 473–475; August, 1958.) A quasi-dc coupling system using a vertical-deflection amplifier input switch providing dc reference pulses for level clamping is described. It is suitable for the range dc–100 mc, and the range of dc shift can be extended indefinitely as far as insulation permits.

621.375.2.132.3 3387

A Direct-Coupled Phase-Splitter—C. Billington. (*Electronic Eng.*, vol. 30, pp. 480–482; August, 1958.) A precision cathode-follower and inverter are described having an output resistance of about 3Ω and a frequency response from dc to beyond 100 kc.

621.375.226:621.396.96 3388

Ring Amplifier—S. Rozenstein and E. Gross. (*Electronic Radio Eng.*, vol. 35, pp. 327–332; September, 1958.) A circuit for amplifying 0.2 μ sec pulses by 110 db in a radar transponder is described. Damped oscillations, produced by the transient response of a tuned circuit, are amplified, and the second half-cycle selected to trigger the transponder. The unit is of small size and has a low power consumption and a fixed internal delay of 0.4 μ sec.

621.375.23 3389

Bootstrap Circuit Technique—A. W. Keen. (*Electronic Radio Eng.*, vol. 35, pp. 345–354; September, 1958.) "The normal amplifier, the bootstrapped amplifier, the cathode-follower and the anode-follower are shown to comprise a set of four circuits related to one another by simple circuit transformations. Three methods of excitation are distinguished. Each circuit may be put into feedback form, and the four basic feedback configurations applicable to bootstrap amplifiers are given. A number of practical examples are described."

621.375.3 3390

Magnetic Amplifiers—D. Katz. (*Bell Lab. Rec.*, vol. 36, pp. 294–297; August, 1958.) The use of magnetic amplifiers as static switching devices is discussed. Switching action is obtained by biasing to saturated or unsaturated states. A binary to quaternary decoder using this principle is described.

621.375.3 3391

Magnetic-Amplifier Design—R. E. Anderson. (*Commun. and Electronics*, no. 36, pp. 160–175; May, 1958.) Commencing with the basic information of power supply frequency, desired gain and time constant, charts are developed to determine the core design, with reference to load voltage and current. With a specified core, additional charts are presented to determine the design of the winding layout.

621.375.3:537.312.62 3392

Superconducting Rectifier and Amplifier—J. L. Olsen. (*Rev. Sci. Instr.*, vol. 29, pp. 537–538; June, 1958.) To avoid heat losses due to heavy-current leads in apparatus at liquid-helium temperatures, a high-voltage ac supply is applied to a transformer which is coupled to the load through a coil of superconducting material. By applying a magnetic field parallel to the axis of the coil a dc component is produced in the load. A current amplification factor of 10 is obtained at 4.2°K using coils of 0.6-mm wire drawn from lead-tin solder. See also 2675 of 1958 (De Vroomen and Van Baarle).

621.375.4 3393

Collector Bias, the Transistor Equivalent of Cathode Bias, and some Applications—R. F. Trehame. (*Proc. IRE, Aust.*, vol. 18, pp. 149–159; May, 1957.) "A self-bias circuit for stabilizing the operating point of a transistor amplifier without unduly decreasing the gain at very low frequencies is discussed. Expressions for the frequency response, stability and input impedance are derived and the application of the circuit to amplifiers, oscillators and active filters is considered."

621.375.4 3394

Diode cuts Transistor Cut-off-Current Drift—H. H. Hoge. (*Electronics*, vol. 31, p. 83; July 18, 1958.) Amplified thermal variations of cut-off current in grounded-emitter amplifiers

can be compensated by connecting a diode, experiencing the same thermal changes and having similar collector/base junction saturation current characteristics, across the transistor base/emitter junction.

621.375.4.024 3395

A Stabilized D.C. Differential Transistor Amplifier—L. Depian and R. E. Smith. (*Commun. and Electronics*, no. 36, pp. 157–159; May, 1958.) Design details and performance characteristics of a circuit which is insensitive to temperature changes. The method employed eliminates feedback and compensating circuits with their attendant complications and disadvantages.

621.375.43 3396

Designing Multiple Feedback Loops—F. H. Blecher. (*Electronic Ind.*, vol. 17, pp. 78–82; April, 1958 and pp. 64–68; May, 1958.) Design considerations applicable to transistors in the common-cathode, common-base or common-emitter connections are discussed. Theorems for determining the gain of any multiple-loop circuit and a stability criterion are given.

621.375.9:538.569.4.029.6 3397

The Saturation Effect in a System with Three Energy Levels—Fain. (See 3420.)

621.375.9:538.569.4.029.64 3398

A Three-Level Solid-State Maser—H. E. D. Scovil. (*Bell Lab. Rec.*, vol. 36, pp. 243–246; July, 1958.) Nonmathematical description of three-level maser operation, including a mechanical analogy. Some constructional details and operating characteristics of a particular model amplifying at 6 kmc are given.

621.375.9.029.64:621.3.011.23:621.314.63 3399

Low-Noise Amplifier—(*Bell Lab. Rec.*, vol. 36, pp. 250–251; July, 1958.) Description of a 6-kmc parametric amplifier using a variable capacitance in the form of a diffused-base Si diode with an active area 0.002 inch in diameter. Advantages and applications of such amplifiers are discussed.

621.376.22:621.314.63 3400

Ring Modulator Reads Low-Level D.C.—E. J. Keonjian and J. D. Schmidt. (*Electronic Ind.*, vol. 17, pp. 86–89; April, 1958.) DC signals in the range 10^{-10} – 10^{-3} A are fed via a logarithmic Si-diode attenuator to a ring modulator and converted to ac, which is amplified and serves as a measure of the dc input. See also 1663 of 1956 (Moody).

GENERAL PHYSICS

535.33-1 3401

The Forty-Eighth Kelvin Lecture: "Infrared Radiation"—G. B. B. M. Sutherland. (*Proc. IEE*, vol. 105, pp. 306–316; July, 1958.) Historical survey with details of applications in the field of infrared spectroscopy. Thirty-three references.

537.122:53.08 3402

Importance of the Faraday to Elemental Constants and Electricity Standards—A. G. McNish and R. D. Huntoon. (*Nature, London*, vol. 181, p. 1194; April 26, 1958.) The ratio e/m can be determined with high accuracy and without uncertainties due to electrical standards and the acceleration of gravity, using the value of the gyromagnetic ratio of the proton determined from precision measurements (see *Nuovo Cim.*, vol. 6, pp. 146–184; 1957) the cyclotron frequency of the proton, and the faraday determined electrochemically.

537.226:621.396.677.8 3403

Anisotropic Effects in Geometrically Isotropic Lattices—Z. A. Kaprielian. (*J. Appl.*

Phys., vol. 29, pp. 1052-1063; July, 1958.) An analysis of the anisotropy produced by an arbitrary ratio of element spacing to wavelength in an artificial lattice dielectric. The "granularity" which is important at high frequencies is considered in detail. See also 1671 of 1956.

537.226.31 **3404**
The Electric Properties of a Dielectric with a Variable Number of Relaxation Centres—N. P. Bogoroditskii, Yu. M. Volokobinskii, and I. D. Fridberg. (*Dokl. Akad. Nauk S.S.S.R.*, vol. 120, pp. 487-490; May 21, 1958.) Expressions are derived for permittivity and of dielectric loss tangent. It is shown that the number of ions and dipoles which give rise to relaxation polarization increases with temperature, leading to an increase of permittivity.

537.311.31 **3405**
Plasma Approach to Metallic Conduction—L. Gold. (*Nature, London*, vol. 181, pp. 1316-1317; May 10, 1958.) Normal and superconductive response in metals may be construed as limiting modes of metallic conduction using a theory of plasma interaction.

537.311.33:539.2:061.3 **3406**
Report on the 5th Course of the International School of Physics of the Italian Physical Society, Varenna, 14th July-3rd August 1957—(*Nuovo Cim.*, vol. 7, pp. 165-736; 1958.) Report of the proceedings of the course on solid-state physics held at the Villa Monastero, Varenna. The text is given of lectures and discussions, including the following:

a) **Optical Properties of Solids**—D. L. Dexter. (pp. 245-286. In English.) Fifty-three references.

b) **The Transition from the Metallic to the Nonmetallic State**—N. F. Mott. (pp. 312-328. In English.)

c) **Electrons and Plasmons**—D. Pines. (pp. 329-352. In English.)

d) **Transport Properties of Solids**—J. M. Ziman. (pp. 353-376. In English.)

e) **Point Imperfections in Solids**—F. Seitz. (pp. 414-443. In English.)

f) **Dislocations in Germanium and Silicon**—H. G. van Bueren, J. Hornstra, and P. Penning. (pp. 646-660. In English.)

g) **Properties of Semiconductors**—H. Y. Fan. (pp. 661-695. In English.)

h) **Semiconducting Compounds**—G. A. Busch. (pp. 696-712. In English.)

i) **Shallow Impurity States in Semiconductors**—W. Kohn. (pp. 713-723. In English.)

j) **Recombination Processes in Semiconductors**—P. Aigrain. (pp. 724-729. In English.)

k) **Semiconductors with Charge Carriers of Low Apparent Mass**—O. Madelung. (pp. 730-736. In German.)

537.311.62 **3407**
The Theory of the Anomalous Skin Effect in Metals—V. P. Silin. (*Zh. eksp. teor. Fiz.*, vol. 33, pp. 1282-1286; November, 1957.) Information concerning the Fermi surface obtained from measurements of surface impedance in the region of the anomalous skin effect does not depend on whether the conduction electrons are considered as a gas or as a degenerate fluid.

537.311.62 **3408**
Skin Effect with Shock Waves—L. Castagnetto. (*Compt. Rend. Acad. Sci., Paris*, vol. 246, pp. 916-918; February 10, 1958.) Approximate formulas are given for the skin effect in a cylindrical conductor traversed by a shock wave.

537.523 **3409**
The Impulse Breakdown Characteristic of a Point/Plane Gap in Air—J. J. Kritzing and G. R. Bozzoli. (*Nature, London*, vol. 181, p. 1259; May 3, 1958.) The influence of the dura-

tion of the impulse wave on the breakdown characteristics for both polarities was investigated for air at a pressure of 62.5 cm Hg and temperature 25°C.

537.533:621.385.029.6 **3410**
The Complex Formulation of the Equations for Two-Dimensional Space-Charge Flow—P. T. Kirstein. (*J. Electronics Control*, vol. 4, pp. 425-433; May, 1958.) The equations satisfied by an electron for congruent space-charge flow are solved using a complex-variable formulation, for a constant magnetic field normal to the flow. Solutions are also obtained in the presence of space charge but with absence of magnetic fields, and for flow along the level lines of a harmonic function.

537.56:538.56 **3411**
Containment of a Fully Ionized Plasma by Radio-Frequency Fields—H. A. H. Boot, S. A. Self, and R. B. R. Shersby-Harvie. (*J. Electronics Control*, vol. 4, pp. 434-453; May, 1958.) A fully ionized plasma is treated as a compressible loss-free dielectric in a RF field. It is shown that there are steady forces which may be used to confine a body of dense plasma in a conducting cavity resonant in a suitable mode. A particular solution, the E_0 cutoff mode, for which extensive numerical calculations have been made is discussed in some detail and interpreted in terms of possible physical experiments.

537.56:538.6:538.56.029.53 **3412**
Investigations on the Occurrence of High-Frequency Oscillations in an Ion Source with Magnetic Guiding Field—H. Kühn. (*Z. Phys.*, vol. 149, pp. 267-275; October 19, 1957.) Oscillations at about 1 mc were observed in H_2 and A, and their amplitude and frequency was measured under various conditions. The effect is interpreted as an acoustic type of plasma oscillation.

537.56:538.63 **3413**
Oscillations in a Plasma with Oriented (D.C.) Magnetic Field—L. Gold. (*J. Electronics Control*, vol. 4, pp. 409-416; May, 1958.) The angular dependence of the double resonances representing coupling of a low-energy plasma and cyclotron oscillations is studied for all orientations of the dc electric and magnetic fields, using a nonlinear phenomenological approach. Conditions favorable for manifestation of these modes are indicated.

538.221 **3414**
Statistics of the Ising Ferromagnet—A. Levitas and M. Lax. (*Phys. Rev.*, vol. 110, pp. 1016-1027; June 1, 1958.) The Ising model is treated by synthesizing a cluster treatment with the spherical model which is used to determine approximately the molecular field acting on the cluster, and the effective interactions between dipoles of the cluster. The method is applied to the square net and to the cubic lattice and the critical temperatures are obtained.

538.221:537.228.4 **3415**
The Use of the Kerr Effect for Studying the Magnetization of a Reflecting Surface—E. W. Lee, D. R. Callaby, and A. C. Lynch. (*Proc. Phys. Soc.*, vol. 72, pp. 233-243; August 1, 1958.) If a domain wall moving in an alternating field crosses a small area illuminated with plane-polarized light, the change in intensity of the reflected light passing through a nearly crossed analyzer can be detected by use of a photomultiplier cell and by amplification of the alternating component of its output signal. Experimental results agree well with theoretical predictions. See also 2441 of 1954 (Fowler and Fryer).

538.222:534.1-8 **3416**
Paramagnetic Centres as Detectors of Ultrasonic Radiation at Microwave Frequencies—C. Kittel. (*Phys. Rev. Lett.*, vol. 1, pp. 5-6; July 1, 1958.) It may be possible to detect microwave phonons generated by an electromechanical or magnetomechanical transducer by observing their effect on the saturation of an electron-spin resonance line. The quantitative aspects of this are estimated.

538.3:535.13 **3417**
The Equations of Electromagnetic Induction—Pham Mau Quan. (*Compt. Rend. Acad. Sci., Paris*, vol. 246, pp. 707-710; February 3, 1958.) The association of Maxwell's electromagnetic equations with Einstein's space-time equations is considered.

538.569.4:535.34:621.372.413 **3418**
Stark-Effect, Resonant-Cavity Microwave Spectrograph—P. H. Verdier. (*Rev. Sci. Instr.*, vol. 29, pp. 646-647; July, 1958.) The construction and use of a cavity for a K-band Stark modulated spectrograph are described. The cavity is a circular cylinder of variable length operating in the TE_{01p} modes. See also 1632 of 1955 (Collier).

538.569.4.029.6:535.33 **3419**
Improvement in Millimetre-Wave Detection—W. E. Tolberg, W. D. Henderson, and A. W. Jache. (*Rev. Sci. Instr.*, vol. 29, pp. 660-661; July, 1958.) A modification of the detector used in mm- λ spectroscopy [2079 of 1954 (King and Gordy)] is described which facilitates the adjustment of the cat's whisker.

538.569.4.029.6:621.375.9 **3420**
The Saturation Effect in a System with Three Energy Levels—V. M. Fain. (*Zh. eksp. teor. Fiz.*, vol. 33, pp. 1290-1294; November, 1957.) Mathematical analysis of the effect of a high-frequency alternating field with given harmonics on a system with three energy levels. Expressions are derived for dielectric constant or permeability applicable to maser operation.

539.2:538.56 **3421**
Spin-Lattice Relaxation Resonances in Solids—H. S. Gutowsky and D. E. Woessner. (*Phys. Rev. Lett.*, vol. 1, pp. 6-8; July 1, 1958.) Preliminary experiments suggest the importance of a spin-lattice relaxation mechanism in certain cases. Possible applications to spin-echo storage devices and to masers are outlined.

539.2:548.0 **3422**
Some Features of the Motion of Rapid Current Carriers in Polar Crystals—Yu. I. Gorkun and K. B. Tolpygo. (*Dokl. Akad. Nauk S.S.S.R.*, vol. 120, pp. 491-495; May 21, 1958.) Investigation of the behavior of polarons (majority current carriers in ionic crystals) with increase of energy.

GEOPHYSICAL AND EXTRATERRESTRIAL PHENOMENA

523.164:621.396.677.3 **3423**
Gain Measurements of Large Antennas used in Interferometer and Cross-Type Radio Telescopes—Little. (See 3339.)

523.164:621.396.677.833 **3424**
Radio Telescope Sees 2 Billion Light Years—C. N. Kington. (*Electronics*, vol. 31, pp. 70-75; June 6, 1958.) Details are given of the drive control system associated with the Jodrell Bank radio telescope. See also 108 of 1958.

523.164:621.396.677.833 **3425**
The Computer and Control for the Telescope at Jodrell Bank. (*Electronic Eng.*, vol. 30, pp. 466-472; August, 1958.) The analog computer and the drive and correction systems which it controls are described.

523.164.3:523.4 3426

Further Observations of Radio Emission from the Planet Jupiter—F. F. Gardner and C. A. Shain. (*Aust. J. Phys.*, vol. 2, pp. 55–69; March, 1958.) Characteristics of radiation at 19.6 mc are described in detail. The radiation appears to be random noise varying rapidly in intensity and its short-term characteristics can be affected markedly by the terrestrial ionosphere. Three main sources of noise are apparent but none can be identified with visual features. The great variability and spectral concentration of the radiation suggests an origin in some form of plasma oscillation in an ionized region having a critical frequency of about 20 mc. See also 406 of 1956 (Shain).

523.164.32:523.74 3427

The Variation of Decimetre-Wave Radiation with Solar Activity—C. W. Allen. (*Mon. Not. R. Astr. Soc.*, vol. 117, pp. 174–188; July, 1957.) "A statistical method is used to segregate the quiet component from the slowly varying component of solar decimetre-wave radiation in the period 1947–54. For this purpose the radiations at frequencies 2800, 1200, and 600 mc have been correlated with sunspot numbers, sunspot areas, and faculae. The mean lives of the various radiations and activities have been estimated and compared. There is an increase of life with decreasing radio frequency. The life of 2800 mc radiation is about the same as sunspots but measurements of the latter show some anomalies. The slowly varying radiation flux is proportional to frequency in the range studied. The quiet sun flux has a small but significant variation with solar activity, the relative change being greater for smaller frequencies. The possibility that this variation may be associated with uncorrelated local sources, such as prominences, is not entirely excluded."

523.165:523.745 3428

Changes in Amplitude of the 27-Day Variation in Cosmic Ray Intensity during the Solar Cycle of Activity—D. Venkatesan. (*Tellus*, vol. 10, pp. 117–125; February, 1958.) The amplitude variation is in general agreement with the changes in solar activity, assessed by the sunspot number, only for the years 1937–1946 and 1952–1955. The poor correlation for the years 1946–1952 may be explained by the changes in the electromagnetic conditions in interplanetary space during the solar cycle.

523.165:523.75 3429

On the Increase in Cosmic Ray Intensity and the Electromagnetic State in Interplanetary Space during the Solar Flare of Feb. 23, 1956—D. Eckhardt. (*Tellus*, vol. 10, pp. 126–136; February, 1958.) A detailed analysis of the onset times of the increase in intensity is used in the study of the electromagnetic state. The existence of deflecting magnetic fields between the sun and the earth is demonstrated. A probable mechanism is discussed whereby flare low-energy cosmic-ray particles could be trapped and guided by a solar beam, which could also have caused the large magnetic storm observed two days after the flare.

523.165:550.385 3430

Geomagnetic Latitude Effect of the Cosmic-Ray Nucleon and Meson Components at Sea Level from Japan to the Antarctic—M. Kodama and Y. Miyazaki. (*Rep. Ionosphere Res. Japan*, vol. 11, pp. 99–115; September, 1957.) Preliminary report on results of measurements made on board the ice-breaker "Sōya" from November, 1956 to April, 1957. The effects of a cosmic-ray storm in the Antarctic are described.

523.5:621.396.11.029.62 3431

A Theoretical Rate-Amplitude Relation in Meteoric Forward Scatter—Hines. (See 3608.)

523.5:621.396.11.029.62 3432

Observations of Angle of Arrival of Meteor Echoes in V.H.F. Forward Scatter Propagations—Endresen, Hagfors, Landmark, and Rødsrud. (See 3609.)

523.5:621.396.11.029.62 3433

The Fading of Long-Duration Meteor Bursts in Forward Scatter Propagation—Landmark. (See 3610.)

523.53 3434

The 1956 Phoenicid Meteor Shower—A. A. Weiss. (*Aust. J. Phys.*, vol. 2, pp. 113–117; March, 1958.) From radio observations at Adelaide six hours before peak activity, the radiant coordinates are estimated to be 15 ± 2 , -55 ± 3 . The radio rate of 30/hour measured on high-sensitivity equipment is much lower than that expected from visual rates of 20 to 100/hour reported 1 to 9 hours later. See also 771 of 1958.

523.75:550.386:621.396.11 3435

Sunspot and Magnetic Activity—A. M. Humby. (*Wireless World*, vol. 64, pp. 435–438; September, 1958.) Unusual features of sunspot and magnetic activity in the years 1950–1957 and their effects on the performance and frequency usage of some HF radio-teletype circuits are examined.

523.78 3436

The Swedish Radio-Scientific Solar Eclipse Expedition to Italy, 1952—S. I. Svensson, G. Hellgren, and O. Perers. (*Acta polyt., Stockholm*, no. 212, 30 pp.; 1957. *Chalmers tek., Högsk. Handl.*, no. 181, 1956.) Preliminary report on observations of the solar eclipse of February 25, 1952. See, e.g., 3378 of 1956 (Minnis).

523.78:551.510.535 3437

Nonuniformity in the Brightness of the Sun's Disk during the Eclipse of 30 June 1954—C. M. Minnis. (*J. Atmos. Terr. Phys.*, vol. 12, pp. 266–271; July, 1958.) The brightness distributions derived from British and Norwegian ionospheric measurements are presented so as to show their underlying similarity. Quantitative data for the most probable distribution are given and a comparison is made with radio noise measurements at 10.7 cm γ during the eclipse. See also 442 of 1957.

550.372(481) 3438

A Survey of Ground Conductivity and Dielectric Constant in Norway within the Frequency Range 0.2–10 Mc/s—K. E. Eliassen. (*Geofys. Publ.*, vol. 19, no. 11, pp. 1–30; 1957.) Measurements were made using the wave tilt method, and a ground conductivity map of Southern Norway has been prepared.

550.385+551.594.5 3439

On the Theory of Magnetic Storms and Aurorae—H. Alfvén. (*Tellus*, vol. 10, pp. 104–116; February, 1958.) It is shown that the non-magnetic beam of ionized gas assumed in the Chapman-Ferraro theory is inconsistent with cosmic-ray observations, and that the main phase of the storm cannot be explained in terms of a nonmagnetic beam. The arguments of Chapman (1356 of 1953) and Cowling (13 of 1943) against the electric field theory are discussed and shown to be invalid.

550.385 3440

Statistical Investigation of Magnetic Crochets at Tamanrasset—F. Duclaux and B. Lepêtre. (*Compt. Rend. Acad. Sci., Paris*, vol. 246, pp. 1243–1245; February 24, 1958.)

550.385 3441

Sub-audible Geomagnetic Fluctuations—H. J. Duffus, P. W. Nasmyth, J. A. Shand, and C. Wright. (*Nature, London*, vol. 181, pp. 1258–

1259; May 3, 1958.) The observations of Duffus and Shand (3076 of 1958) have been extended to cover the frequency range 0.1–30 cps. Records obtained at a portable subsidiary station about 200 miles from the main station near Victoria, B.C., in the same magnetic latitude, showed no phase shift of the normal day-time oscillations.

550.385 3442

Large-Amplitude Hydromagnetic Waves above the Ionosphere—A. J. Dessler. (*Phys. Rev. Lett.*, vol. 1, pp. 68–69; July 15, 1958.) The hydromagnetic-wave velocity is calculated as a function of altitude. There are two regions where the wave velocity changes very rapidly with altitude and it is concluded that hydromagnetic waves above the ionosphere have an amplitude greater than the geomagnetic fluctuations they produce at the surface of the earth. See also 3077 of 1958.

550.385.1:523.75 3443

Method of Magnetic-Storm Forecasting from the Activities of Flares accompanied by Solar Radio Noise Outbursts—K. Sinno. (*Rep. Ionosphere Res. Japan*, vol. 11, pp. 195–204; December, 1957.) A statistical study indicates that solar flares accompanied by 200-mc radio noise bursts have a close correlation with terrestrial magnetic storms. See also 446 of 1958.

550.385.4:523.165 3444

On the Magnetic Clouds responsible for Variations of Cosmic-Ray and Geomagnetic Field—M. Hirono. (*Rep. Ionosphere Res. Japan*, vol. 11, pp. 205–228; December, 1957.) Discussion of the mechanism suggested by Morrison (*Phys. Rev.*, vol. 101, pp. 1397–1404; February 15, 1956) by which large ionized gas clouds carrying tangled magnetic fields are emitted from the sun and modulate the galactic cosmic rays reaching the earth. It is shown to be more probable that smaller magnetic clouds are intermittently ejected from the sun and slowed down by the interplanetary gas. The velocity of accompanying unmagnetized streams is unaffected, and the different velocities account for the observed initial and main phases of terrestrial magnetic storms; the model also explains some solar cosmic ray phenomena. Thirty-nine references.

550.389.2:621.396.11 3445

Radio Studies during the International Geophysical Year 1957–8—W. J. G. Beynon. (*J. Brit. IRE*, vol. 18, pp. 401–412; July, 1958. Discussion, pp. 412–416.) Studies are discussed under five headings: a) vertical soundings, b) ionospheric drift measurements, c) backscatter, d) radio noise and atmospheric studies, and e) rockets and satellites. The history, program and organization of the I.G.Y. are briefly outlined.

550.389.2:629.19 3446

Theoretical Analysis of Doppler Radio Signals from Earth Satellites—W. H. Guier and G. C. Weiffenbach. (*Nature, London*, vol. 181, pp. 1525–1526; May 31, 1958.) The analysis is briefly described and its application to the calculation of the orbits of two satellites (Sputnik I and Explorer I) from isolated observations made at one station is given.

550.389.2:629.19 3447

Observations of the U.S. Satellites Explorers I and III by C.W. Reflection—J. D. Kraus, R. C. Higgy and J. S. Albus. (*Proc. IRE*, vol. 46, p. 1534; August, 1958.) The passage of satellites Explorer I and III may be detected by the increased signal strength of WWV as a result of ionization from the satellite paths. See also 1724 of 1958 (Kraus).

550.389.2:629.19 3448

Continuous Phase-Difference Measurements of Earth Satellites—J. W. Herbstreit

and M. C. Thompson, Jr. (PROC. IRE, vol. 46, p. 1535; August, 1958.) Two similar receivers are used, operated from a common local oscillator. The phase-meter compares the AF tones from the two receivers. See also 234 of 1956.

550.389.2:629.19 3449

On the Interpretation of the Doppler Effect from Senders in an Artificial Satellite—K. Weekes. (*J. Atmos. Terr. Phys.*, vol. 12, pp. 335–338; July, 1958.) The Doppler effect is simply related to the angle of incidence of the transmitted signal if the geomagnetic field is ignored, otherwise the relationship is complex, and an investigation of the actual ray-paths is necessary even for the deduction of approximate numerical values.

550.389.2:629.19:551.510.535 3450

The Effect of the Ionosphere on the Doppler Shift of Radio Signals from an Artificial Satellite—F. H. Hibberd. (*J. Atmos. Terr. Phys.*, vol. 12, pp. 338–340; July, 1958.) Application of Snell's law to a ray passing through a spherically stratified ionosphere to a receiver on the ground leads to a relation between Doppler shift and angle of incidence at the ground.

551.510.3 3451

High-Atmosphere Densities—M. Nicolet. (*Science*, vol. 127, pp. 1317–1320; June 6, 1958.) Models of the upper atmosphere are modified to allow for diffusion and other factors in order to conform to the results obtained from satellite observations.

551.510.53:550.38:523.165 3452

Distortion of the Magnetic Field in the Outer Atmosphere due to the Rotation of the Earth—K. Maeda. (*Rep. Ionosphere Res. Japan*, vol. 11, pp. 116–129; September, 1957.) Assuming a cavity surrounding the earth, caused by the earth's revolution, the equations of the fields inside and outside this cavity imply a westward shift of the dip equator in the outer atmosphere, in agreement with cosmic-ray evidence. See e.g., 3721 of 1956 (Simpson, *et al.*).

551.510.535 3453

Anomalies in Ionosonde Records due to Travelling Ionospheric Disturbances—L. H. Heisler. (*Aust. J. Phys.*, vol. 2, pp. 79–90; March, 1958.) Anomalies in ionosonde records of the *F* region during the passage of traveling disturbances are classified into four main types. The diurnal and seasonal variation of their occurrence is discussed and it is suggested that the ion distribution at a height of 200 km governs the type of anomaly observed. See also 1434 of 1957 (Munro and Heisler).

551.510.535 3454

Travelling Ionospheric Disturbances in the *F* Region—G. H. Munro. (*Aust. J. Phys.*, vol. 2, pp. 91–112; March, 1958.) Data obtained from April, 1948, to March, 1957, on the horizontal movements of the disturbances are analyzed for a single radio frequency. The monthly means of direction show a seasonal change from 30° in winter to 120° in summer with a small change in mean speed from 8 km/min to 7 km/min respectively.

551.510.535:523.3 3455

Measurement of the Ionospheric Faraday Effect by Radio Waves Reflected from the Moon—F. B. Daniels and S. J. Bauer. (*Nature, London*, vol. 181, pp. 1392–1393; May 17, 1958.) Continuous waves at 151.11 mc were transmitted from Belmar, N. J., and received at Urbana, Ill., after reflection from the moon. From 2333–0600 CST the change in total electron content deduced from measurements made during the night of January 8–9, 1958, was about 2.2 times the change computed for a parabolic layer from vertical-incidence recordings at the transmitter site.

551.510.535:523.72 3456

The Effect of Certain Solar Radiations on the Lower Ionosphere—R. E. Houston, Jr. (*J. Atmos. Terr. Phys.*, vol. 12, pp. 225–235; July, 1958.) "An electron density distribution in the *D* and *E* regions of the ionosphere is computed. Lyman alpha, Lyman beta, the Lyman continuum and X-radiations are considered. The resulting electron distribution is used to compute parameters which may then be compared with data from rocket and long wave radio experiments. In general, there is good agreement between experimental results and the values predicted by the model."

551.510.535:523.75 3457

On the Ionospheric Current System of the Geomagnetic Solar Flare Effect (S.F.E.)—H. Volland and J. Taubenheim. (*J. Atmos. Terr. Phys.*, vol. 12, pp. 258–265; July, 1958.) The analysis of 16 magnetograms obtained at Niemegk (near Berlin) between 1951 and 1957 shows that the s.f.e. current system is independent of the *S_q* system and situated at a lower level. Contributions to the geomagnetic s.f.e. apparently come from both the *D* and *E* regions. See also 3866 of 1957 (Taubenheim).

551.510.535:523.78 3458

The Interpretation of Changes in the *E* and *F*-Layers during Solar Eclipses—C. M. Minnis. (*J. Atmos. Terr. Phys.*, vol. 12, pp. 272–282; July, 1958.) Results obtained during a series of eclipses support an interpretation of ionospheric changes in terms of the response of a Chapman layer to the obscuration of a solar disk where localized sources of ionizing radiation are superposed on a uniformly bright background. An alternative hypothesis of a uniform disk and a complex layer with two different species of ion does not adequately explain observed characteristics. Experimental results indicate that errors due to layer tilts are probably not important. See also 3437 above.

551.510.535:551.557 3459

Method of Measuring Ionospheric Winds by Fading at Spaced Receivers—R. B. Banerji. (*J. Atmos. Terr. Phys.*, vol. 12, pp. 248–257; July, 1958.) Current statistical methods of measurement are critically reviewed and compared. As a result a method is suggested that may be less laborious than the autocorrelation methods but of comparable accuracy. See, e.g., 3216 of 1954 (Ratcliffe).

551.510.535:621.396.11 3460

On the Bearing of Ionospheric Radio Waves—K. Miya, M. Ishikawa, and S. Kanaya. (*Rep. Ionosphere Res. Japan*, vol. 11, pp. 130–144; September, 1957.) Systematic measurements of bearings obtained by means of special DF equipment [465 of 1958 (Miya, *et al.*)] are analyzed, and fluctuations are interpreted with regard to propagation modes and distance. When the great-circle m.u.f. exceeds the signal frequency the mean bearing coincides with the direction of the main beam of the transmitter aerial, but deviates considerably when the great-circle MUF falls below the signal frequency. The changes are attributed to a major deviation from the great-circle path combined with a final scatter hop from continental land masses. Deviation of antipodal signal bearings are explained assuming that the signals follow paths of low absorption ("night zones").

551.510.535:621.396.11:621.317.799 3461

An Automatic Recorder For Measuring Ionospheric Absorption—S. C. Mazumdar. (*J. Inst. Telecommun. Eng., India*, vol. 4, pp. 81–86; March, 1958.) Ionospheric absorption is deduced from the ratio of the amplitudes of singly and doubly reflected vertical incidence pulses. The two pulses are separated by adjustable gates and applied to two logarithmic amplifiers followed by a difference circuit

operating a chart recorder. In the absence of a second reflection a local reference pulse can be used, the system being calibrated subsequently. See 1444 of 1957 (Mittra and Mazumdar).

551.510.535:621.396.11.029.45/.5 3462

Low-Frequency Reflection in the Ionosphere—Poeverlein. (See 3604.)

551.510.536 3463

The Transition from the Ionosphere to Interplanetary Space—D. E. Blackwell. (*Nature, London*, vol. 181, pp. 1237–1238; May 3, 1958.) Report of a discussion held by the Royal Astronomical Society in London, February 21, 1958, including five short talks concerning the solar corona, zodiacal light, radio echoes from the moon, earth-satellite observations, and AF atmospherics.

551.551:551.508.822 3464

Free-Air Turbulence—A. D. Anderson. (*J. Met.*, vol. 14, pp. 477–494; December, 1957.) Measurements of the altitude distribution between 3000 and 18,300 m of layers of turbulence made by means of a "gustsonde" incorporating a VHF transmitter are analyzed.

551.594.21 3465

Thunderstorm Charge Separation—S. E. Reynolds, M. Brook and M. F. Gourley. (*J. Met.*, vol. 14, pp. 426–436; October, 1957.) Laboratory experiments show that charge separation may arise from the collision between graupel pellets and ice crystals, from friction between ice formations at different temperatures or with different amounts of contamination, and from the resolidification of a liquid layer in contact with ice.

551.594.5:621.396.11.029.6 3466

Low-Latitude Reflection from the Aurora Australis—T. J. Seed and C. D. Ellyett. (*Aust. J. Phys.*, vol. 2, pp. 126–129; March, 1958.) Observations of radar reflections for the period March–June, 1957, are reported. Records of radar, visual and geomagnetic observations for one day are compared.

551.594.6:621.396.11.029.45 3467

Velocity of Propagation of Electromagnetic Waves at Audio Frequencies—Al'pert and Borodina. (See 3605.)

LOCATION AND AIDS TO NAVIGATION

621.396.93 3468

Methods and Installations for Long-Distance Radio Navigation—W. Stanner. (*Elektrotech. Z., Ed. A.*, vol. 79, pp. 322–329; May 1, 1958.) A review of the principal present-day systems including Loran, Consol and Decra.

621.396.93 3469

Improvements in H.F. Direction Finding by Automatic Time Averaging—J. F. Hatch and D. W. G. Byatt. (*Marconi Rev.*, vol. 21, pp. 16–29; 1958.) Equipment is described for use with CW or ICW signals which gives automatically the mean bearing averaged over a range of time intervals. The improvement is assessed by comparison with simultaneous bearings observed on twin-channel CRDF equipment.

621.396.93(94) 3470

The Australian D.M.E. System—E. Stern. (*Proc. IRE, Aust.*, vol. 18, pp. 318–327; September, 1957.) Description of the development and operation of the system. See 3471 below.

621.396.93.029.62 3471

Echo Interference in a 200-Mc/s Double-Pulse D.M.E. System—B. R. Johnson. (*Proc. IRE, Aust.*, vol. 18, pp. 309–317; September, 1957.) In DME systems such as the Australian system using double-pulse interrogation coding as a means of channel selection, echo interfer-

ence may cause a) interrogation of off-channel beacons, b) incorrect range indication, or c) masking of beacon identification code. Theoretical analysis and experimental work indicate what type of reflectors may be troublesome, and how echo interference can be minimized.

621.396.933 3472

Factors in the Design of Airborne Doppler Navigation Equipment—E. G. Walker. (*J. Brit. IRE*, vol. 18, pp. 425-442; July, 1958. Discussion, pp. 442-444.) "The paper describes the use of a Doppler-sensor of aircraft component-velocities as an input for self-contained dead-reckoning navigation. Choice of radio frequencies, beam configuration, radiated power and other system parameters is discussed and some basic quantitative expressions derived. Design features of the individual units of the sensor are given and requirements of computer and heading-reference outlined. System accuracy is discussed and the heading information is shown to be the factor presently limiting system performance."

621.396.933.1:621.396.824 3473

Sudden Changes in Bearing Indication on Medium-Wave Four-Course Radio Ranges using Cathode-Ray Direction-Finders—A. R. Wendlinger. (*Elektronische Rundschau*, vol. 12, pp. 10-12; January, 1958.) Experimental investigations of the Stavanger effect show that it is due to interference at the receiver between signals emitted by two different radio beacons operating at almost identical frequencies.

621.396.96 3474

The Influence of Atmospheric Conditions on Radar Performance—J. A. Saxton. (*J. Inst. Nav.*, vol. 11, pp. 290-303; July, 1958.) The effects of gaseous absorption and of various forms of precipitation upon the performance of radars at 3 cm λ are reviewed. Heavy widespread rain can cause serious reduction in range. The effects of superrefraction are discussed, and it is shown how skip effects can occur.

621.396.96 3475

A 3-cm Airport Control Radar System—F. W. Garrett. (*Marconi Rev.*, vol. 21, no. 128, pp. 3-15; 1958.)

621.396.96 3476

Four Ways to Simulate Radar Targets—J. I. Leskinen. (*Electronics*, vol. 31, pp. 82-86; June 6, 1958.) Pulses are generated to simulate azimuth, elevation and range of targets moving at speeds up to 2400 knots. Land and sea clutter effects are also produced.

621.396.96:621.375.226 3477

Ringup Amplifier—Rozenstein and Gross. (See 3388.)

621.396.969.33 3478

The Planning of Shore-Based Radar Installations for Marine Navigation—H. Bürkle. (*Telefunken Ztg.*, vol. 30, pp. 236-245; December, 1957. English summary, p. 287.) Factors governing the choice of site and coverage and transmitter and antenna characteristics are examined. Avoidance of interference from neighboring stations, and systems of transmitter control are also considered.

MATERIALS AND SUBSIDIARY TECHNIQUES

535.215 3479

Photoconductivity of Zinc Selenide Crystals and a Correlation of Donor and Acceptor Levels in II-VI Photoconductors—R. H. Bube and E. L. Lind. (*Phys. Rev.*, vol. 110, pp. 1040-1049; June 1, 1958.) Photosensitive crystals of ZnSe were prepared by incorporating suitable proportions of group-VII donors and either group-I or group-V acceptors in crystals pre-

pared from the vapor phase. Photoconductivity phenomena characteristic of other group II-VI photoconductors were also found for ZnSe.

535.215 3480

Photo-effects with Anodic Oxide Layers on Tantalum and Aluminium—W. C. van Geel, C. A. Pistorius, and P. Winkel. (*Philips Res. Rep.*, vol. 13, pp. 265-276; June, 1958.) The photoelectric properties of the system Ta/Ta₂O₅/electrolyte during irradiation with ultraviolet light are investigated, and an attempt is made to explain the observed phenomena by assuming that the work function for Ta/Ta₂O₅ is smaller than that for electrolyte/Ta₂O₅.

535.37 3481

Phosphorescence and Fluorescence Quantum Yield Ratios as related to the Position of the Fluorescence Spectrum—V. V. Zelinskii and V. P. Kolobkov. (*Dokl. Akad. Nauk S.S.S.R.*, vol. 119, pp. 922-925; April 11, 1958.)

535.37 3482

Investigations in the CuGaS₂-ZnS and AgGaS₂-ZnS Systems—E. F. Apple. (*J. Electrochem. Soc.*, vol. 105, pp. 251-255; May, 1958.)

535.37:546.472.21 3483

Some Remarks on the "Self-Activation" of ZnS—E. A. Schwager and A. Fischer. (*Z. Phys.*, vol. 149, pp. 345-346; October 19, 1957.) The effect is interpreted as a shift of Schottky-type defect equilibrium according to the conditions of phosphor preparation.

535.37:546.472.21 3484

A Sensitive Method of Detecting Lead, and the Inclusion of Lead in Zinc Sulphide—E. A. Schwager and A. Fischer. (*Z. Phys.*, vol. 149, pp. 347-352; October 19, 1957.) Activation of ZnS by Pb is discussed.

535.376 3485

The Effect of Electric Fields on Scintillations in Crystalline Zinc Sulphide—G. F. Alfrey and K. N. R. Taylor. (*J. Electronics Control*, vol. 4, pp. 417-424; May, 1958.) In electroluminescent crystals brightness is reduced when α particles are incident on the negative electrode. Observations have been interpreted in terms of a cathode barrier in vns which changes in thickness with frequency, the variation being considered to be a change in dielectric constant. Results agree with earlier work [782 of 1956 (Ince and Oatley)] and are supported by observations of the electroluminescence threshold voltage.

535.376:621.385.832 3486

Electron Excitation of Bilayer Screens—L. R. Koller and H. D. Coghill. (*J. Appl. Phys.*, vol. 29, pp. 1064-1066; July, 1958.) "The control of the color of the luminescence of thin transparent superimposed phosphor films when excited by electron beams of varying voltage is discussed. The quantitative relations are found to be in agreement with a theory based on the laws of electron penetration and scattering."

537.226/.228.1:546.431.824-31 3487

Some Studies on the Ternary System (Ba-Pb-Ca)TiO₃—T. Ikeda. (*J. Phys. Soc. Japan*, vol. 13, pp. 335-340; April, 1958.) The phase diagram for the system is investigated while the Ca concentration is increased, and it is shown that the ferroelectric and tetragonal phase changes to the orthorhombic structure of CaTiO₃, passing through cubic and pseudocubic phases. The dielectric, piezoelectric and mechanical properties of the system are also examined.

537.226/.227:546.431.824-31 3488

Barkhausen Pulses in Barium Titanate—

A. G. Chynoweth. (*Phys. Rev.*, vol. 110, pp. 1316-1332; June 15, 1958.) An investigation of the Barkhausen pulses that occur during polarization reversal. The pulse shapes and in particular their heights and rise times have been studied as a function of the crystal thickness and the applied field strength. The observations are not consistent with the usual jerky domain-wall motion models for the generation of Barkhausen pulses. It is suggested that the pulses could represent the nucleation and initial stages of growth of new spike-shaped domains extending along the c axis, and that the fixed numbers of pulses given by a crystal would then indicate a definite number of nucleating sites on the crystal surfaces.

537.226/.227:546.431.824-31 3489

Decay Effects in Barium Titanate Ceramics—H. L. Allsopp. (*Phil. Mag.*, vol. 2, pp. 1100-1102; September, 1957.) Variations of dielectric and electromechanical properties following the application and removal of a strong alternating field are described.

537.226/.227:546.431.824-31 3490

Electron Spin Resonance in Single Crystals of BaTiO₃—W. Low and D. Shaltiel. (*Phys. Rev. Lett.*, vol. 1, pp. 51-52; July 15, 1958.) The very intense spectrum observed at 3 cm λ is attributed to the ferroelectric state of BaTiO₃ and not to any paramagnetic impurity.

537.226:546.824-31 3491

Dielectric Losses in TiO₂ Single Crystals—J. Van Keymeulen. (*Naturwissenschaften*, vol. 45, p. 56; February, 1958. In English.)

537.227 3492

The Polarization Reversal Process in Ferroelectric Single Crystals—M. Prutton. (*Proc. Phys. Soc.*, vol. 72, pp. 307-308; August 1, 1958.)

537.227 3493

New Room-Temperature Ferroelectric—R. Pepinsky, K. Vedam, and Y. Okaya. (*Phys. Rev.*, vol. 110, pp. 1309-1311; June 15, 1958.) The neutral-salt complex with glycine (NH₃CH₂COOH)·MnCl₂·2H₂O is found to be ferroelectric from low temperatures to +55°C. Details of measurements on this salt are given.

537.227 3494

Ferroelectric and Optical Properties of Na(K-NH₄)-Tartrate Mixed Crystals—Y. Makita and Y. Takagi. (*J. Phys. Soc. Japan*, vol. 13, pp. 367-377; April, 1958.) In 90.5 per cent NaNH₄ tartrate crystals three kinds of polymorphic modification have been found: a) a ferroelectric phase with spontaneous polarization along the a axis; b) a ferroelectric phase with polarization along the b axis; c) a paraelectric phase. The complete phase diagram of the system is examined.

537.311.3:539.23 3495

Remarks on some Electrical Properties of Very Thin Films of Silver—C. Uny and N. Nifontoff. (*Compt. Rend. Acad. Sci., Paris*, vol. 246, pp. 906-909; February 10, 1958.) Techniques used in the preparation of regular and stable thin films are noted, and measurements of resistance variation with time and with current are reported. See also 2167 of 1957.

537.311.33 3496

Statistics of Compensated Divalent Impurities in Semiconductors—W. Mercuroff. (*Compt. Rend. Acad. Sci., Paris*, vol. 246, pp. 1175-1177; February 24, 1958.) The introduction of compensating monovalent impurity centers considerably modifies the variation in the number of free carriers as a function of temperature. Analytical results have been confirmed by experiments on Zn-doped Ge compensated by Sb.

- 537.311.33 3497**
Theory of an Experiment for Measuring the Mobility and Density of Carriers in the Space-Charge Region of a Semiconductor Surface—R. L. Petritz. (*Phys. Rev.*, vol. 110, pp. 1254–1262; June 15, 1958.) Two models are considered: a) a single crystal composed of two regions, a surface region of thickness of the order of a Debye length and a bulk region, and b) a single crystal with continuous variation of the potential in the direction perpendicular to the surface. Rigorous expressions are derived for the Hall coefficient and magnetoresistance.
- 537.311.33 3498**
Oxides of the 3d Transition Metals—F. J. Morin. (*Bell Sys. Tech. J.*, vol. 37, pp. 1047–1084; July, 1958.) An examination of the magnetic, electrical and optical properties leads to a tentative energy-band scheme for the oxides of scandium, titanium and vanadium. The remaining 3d metal oxides do not have a conduction band, and an energy level scheme for these is calculated from electrostatics. Forty-seven references.
- 537.311.33 3499**
Compound Semiconductors—H. P. R. Frederikse. (*J. Metals, New York*, vol. 10, pp. 346–350; May, 1958.) "A survey of the characteristics of compound semiconductors as deduced from measurements of their mechanical, optical, electrical, magnetic, and thermal properties."
- 537.311.33 3500**
Solid Solution in $Al^{III}B^V$ Compounds—J. C. Wooley and B. A. Smith. (*Proc. Phys. Soc.*, vol. 72, pp. 214–223; August 1, 1958.) Investigations show that in most of the compounds considered, complete solid solution can be obtained throughout the whole range of composition under special conditions of temperature and annealing time.
- 537.311.33 3501**
Adsorption and Charge Transfer on Semiconductor Surfaces—H. J. Krusemeyer and D. G. Thomas. (*Phys. Chem. Solids*, vol. 4, nos. 1/2, pp. 78–90; 1958.) A theoretical evaluation of the concentration of ions and neutral atoms adsorbed on a semiconductor surface, from a mixture of two gases, one giving positive, the other negative, adions. Numerical results are calculated for semiconductors such as ZnO with a large forbidden gap at temperatures below the intrinsic range.
- 537.311.33 3502**
Space-Charge Calculations for Semiconductors—R. Seiwatz and M. Green. (*J. Appl. Phys.*, vol. 29, pp. 1034–1040; July, 1958.) A derivation of the general equation relating the electric field at the semiconductor surface to the electrostatic potential difference across the space charge region. The treatment considers degenerate free carrier distributions and partial ionization of impurities.
- 537.311.33 3503**
Sweep-Out Effects in the Phase-Shift Method of Carrier-Lifetime Measurements—N. B. Grover and E. Harnick. (*Proc. Phys. Soc.*, vol. 72, pp. 267–269; August 1, 1958.) The particular case of thin rectangular filaments with ohmic contacts and low-level sinusoidally modulated illumination is considered with a view to determining an upper limit for the value of the applied field consistent with negligible sweep-out effects.
- 537.311.33 3504**
Infrared and Microwave Modulation using Free Carriers in Semiconductors—A. F. Gibson. (*J. Sci. Instrum.*, vol. 35, pp. 273–278; August, 1958.) The failures and successes of the classical Drude-Zener theory in relation to experimental results are discussed. Methods are described for modulating the conductivity of a semiconductor and for applying these techniques to the study of its optical and microwave properties.
- 537.311.33:061.3 3505**
Report on the Second Symposium on the Physics of Semiconductors—F. Herman. (*Phys. Chem. Solids*, vol. 2, pp. 72–82; March, 1957.) Summary of papers presented at a symposium in Washington, D. C., October 24–26, 1956, covering work on conduction mechanisms, the effect of magnetic fields, and investigations of paramagnetic resonance.
- 537.311.33:538.569.4 3506**
Observation of Microwave Cyclotron Resonance by Cross Modulation—H. J. Zeiger, C. J. Rauch, and M. E. Behrndt. (*Phys. Rev. Lett.*, vol. 1, pp. 59–60; July 15, 1958.) The sample was placed in the high E-field region of a microwave cavity, the resonance peaks being observed by detecting changes in dc resistance of the sample. The microwave power applied was amplitude-modulated at 260 cps and cross-modulation was observed on samples of pure Ge and p-type InSb.
- 537.311.33:538.63 3507**
Variation of Hall Mobility of Carriers in Nondegenerate Semiconductors with Electric Field—M. S. Sodha and P. C. Eastman. (*Phys. Rev.*, vol. 110, pp. 1314–1316; June 15, 1958.) An expression is obtained for the Hall mobility applicable in a large range of fields and non-Maxwellian distribution of velocities of carriers.
- 537.311.33:538.63 3508**
Hall and Transverse Magnetoresistance Effects for Warped Bands and Mixed Scattering—A. C. Beer and R. K. Willardson. (*Phys. Rev.*, vol. 110, pp. 1286–1294; June 15, 1958.) The transport integrals for warped bands were evaluated for relaxation times determined by mixed scattering from acoustic phonons and ionized impurities. Hall and transverse magnetoresistance coefficients were calculated for parameters characteristic of the degenerate valence bands in Ge and Si, the results being consistent with experimental observations.
- 537.311.33:538.63 3509**
The Change of Carrier Concentration in the Simple Semiconductors with Static Magnetic Field—Y. Uemura and M. Inoue. (*J. Phys. Soc. Japan*, vol. 13, pp. 377–381; April, 1958.) Three solutions are considered depending on the trapping-center concentration: a) with distinct trapping levels the carrier concentration n decreases with the magnetic field H ; b) with sufficient levels to form an impurity band whose width is less than kT , n increases or decreases depending on the effective carrier mass; c) n increases with H for large effective carrier mass when the width of the impurity band is greater than kT .
- 537.311.33:[546.28+546.289] 3510**
The Magnetic Susceptibility and Effective Mass of Charge Carriers in Silicon and Germanium—D. Geist. (*Naturwissenschaften*, vol. 45, pp. 33–34; January, 1958.) Preliminary report on measurements of susceptibility at constant temperatures, from which any temperature dependence of the effective mass can be determined.
- 537.311.33:546.28 3511**
Ion Pairing in Silicon—J. P. Maita. (*Phys. Chem. Solids*, vol. 4, nos. 1/2, pp. 68–70; 1958.) "The occurrence of ion pairing in Si is demonstrated. The pairing process is used to determine the diffusivity of Li in Si at low temperatures and the distance of closest approach between the ions forming the pair."
- 537.311.33:546.28 3512**
Lifetime in p-Type Silicon—J. S. Blakemore. (*Phys. Rev.*, vol. 110, pp. 1301–1308; June 15, 1958.) Lifetime is measured as a function of excess electron density in the temperature range 200–400°K. A stronger dependence is found at electron densities $<10^{12}\text{cm}^{-3}$ than at larger densities. The data are discussed in terms of two separate recombinative levels.
- 537.311.33:546.28 3513**
Magnetic Properties of N-Type Silicon—E. Sonder and D. K. Stevens. (*Phys. Rev.*, vol. 110, pp. 1027–1034; June 1, 1958.) The magnetic susceptibility of n-type Si samples with a wide range of donor concentrations has been measured as a function of temperature from 3°K to 300°K. By utilizing conduction-electron concentrations obtained from Hall coefficient measurements on comparison specimens over the range 50°K–400°K, the contributions to the susceptibility arising from the conduction electrons and electrons trapped on donor atoms have been analyzed. In the upper range of temperature the diamagnetic contribution of conduction electrons is dominant and is consistent with the model of six energy minima in the conduction band. However, comparison of the squared reciprocal mass ratio with that obtained from cyclotron-resonance experiments reveals that the former is appreciably smaller than the latter.
- 537.311.33:546.28 3514**
Effect of Dislocations on Breakdown in Silicon p-n Junctions—A. G. Chynoweth and G. L. Pearson. (*J. Appl. Phys.*, vol. 29, pp. 1103–1110; July, 1958.) A description of experiments providing definite correlations between the light-emission patterns at breakdown and dislocations, the latter being revealed by etching. The possible explanations of this effect are discussed. See e.g., 3527 of 1957 (Chynoweth and Pearson).
- 537.311.33:546.28 3515**
Electron-Bombardment Damage in Silicon—G. K. Wertheim. (*Phys. Rev.*, vol. 110, pp. 1272–1279; June 15, 1958.) It is shown that the bombardment imperfections consist of sites containing at least two electrically active point defects. The relation between these sites and the energy levels in the forbidden gap found in an earlier investigation is established. See also 2807 of 1957.
- 537.311.33:546.28 3516**
Method for the Detection of Dislocations in Silicon by X-Ray Extinction Contrast—J. B. Newkirk. (*Phys. Rev.*, vol. 110, pp. 1465–1466; June 15, 1958.)
- 537.311.33:546.28 3517**
Sintering Method for Semiconductor Material—G. K. Gaulé, J. T. Breslin, and J. R. Pastore. (*Rev. Sci. Instrum.*, vol. 29, pp. 565–567; July, 1958.) A sintering process is described for forming small grains of pure Si into rods suitable for feeding a crystal-growing apparatus [see e.g., 3255 of 1954 (Keck, et al.)]. The rods are sintered by application of pressure, alternating current and a RF field without using a binder.
- 537.311.33:546.28 3518**
Control of Surface Concentration in the Diffusion of Phosphorus in Silicon—M. J. Coupland. (*Nature, London*, vol. 181, pp. 1331–1332; May 10, 1958.) Desired values of surface concentration over the range 5×10^{18} – 5×10^{19} atoms/cm² are obtained by controlling the phosphorus vapor pressure in closed a evacuated tube, one end of which, containing Si slices, is held in a diffusion furnace, while the other, containing yellow phosphorus, is maintained at temperatures in the range -30°C to $+35^\circ\text{C}$.

- 537.311.33:546.28 3519
The Interaction of Oxygen with Clean Silicon Surfaces—J. T. Law. (*Phys. Chem. Solids*, vol. 4, nos. 1/2, pp. 91–100; 1958.)
- 537.311.33:546.28:538.632 3520
The Electrical Conductivity and Hall Effect of Silicon—E. H. Putley and W. H. Mitchell. (*Proc. Phys. Soc.*, vol. 72, pp. 193–200; August 1, 1958.) Measurements have been made in the temperature range 20°–500°K on single crystals of Si with extrinsic carrier concentrations between 2 and $5 \times 10^{15} \text{ cm}^{-3}$ to estimate the purity of the material and to study the Hall mobility. Mobilities of electrons and holes are greater than previously observed [e.g., 2184 of 1957 (Cronmeyer)].
- 537.311.33:546.289 3521
Predicted Intervalley Scattering Effects in Germanium—W. Shockley. (*Phys. Rev.*, vol. 110, pp. 1207–1208; June 1, 1958.) Two methods for studying intervalley scattering effects are described. One is the study of the admittance of an n - p junction at high frequencies; the other method uses an n - p - n transistor with suitable properties.
- 537.311.33:546.289 3522
Impact Ionization of Impurities in Germanium—N. Sclar and E. Burstein. (*Phys. Chem. Solids*, vol. 2, pp. 1–23; March, 1957.) The low-temperature electrical breakdown effect is investigated experimentally as a function of temperature, magnetic field, background radiation, type and concentration of impurities, geometry, surface effects, orientation of the specimens and time dependence. The effect is attributed to the impact ionization of impurities by free charge carriers, and a mean-value theory is developed for the critical breakdown field. See also 1796 of 1957 (Sclar).
- 537.311.33:546.289 3523
Effect of the Impurity Band in Germanium Doped with Zinc, at Very Low Temperatures—W. Mercuroff. (*Compt. Rend. Acad. Sci., Paris*, vol. 246, pp. 1013–1015; February 17, 1958.) At low temperatures, Hall effect and conductivity in samples of Ge, heavily doped with Zn and compensated with Sb, were found to vary with the applied electric field.
- 537.311.33:546.289 3524
The Effect of Ion Pair and Ion Triplet Formation on the Solubility of Lithium in Germanium—Effect of Gallium and Zinc—H. Reiss and C. S. Fuller. (*Phys. Chem. Solids*, vol. 4, pp. 58–67; 1958.) Theoretical predictions of the effect of ion pairing or association on solubility are confirmed. By taking account of ion association effects a more accurate curve for the solubility of Li in undoped Ge is obtained.
- 537.311.33:546.289 3525
Preparation and Regeneration of Clean Germanium Surfaces—S. P. Wolsky. (*J. Appl. Phys.*, vol. 29, pp. 1132–1133; July, 1958.) A summary of a) a modified method designed to improve the cleaning efficiency of the ion bombardment process, and b) thermal restoration effects in Ge surfaces exposed to oxygen.
- 537.311.33:546.289 3526
Temperature Dependence of Point-Contact Injection Ratio in Germanium—D. Gerlich. (*Proc. Phys. Soc.*, vol. 72, pp. 264–267; August 1, 1958.) A method is described for the measurement of point-contact injection ratio by direct compensation. Results are given for n and p -type material for the temperature range 150–350°K. See also 1821 of 1957.
- 537.311.33:546.289:538.63 3527
Magneto-surface Experiments on Germanium—J. N. Zemel and R. L. Petritz. (*Phys. Rev.*, vol. 110, pp. 1263–1271; June 15, 1958.) Ambient-induced changes in the conductivity, Hall coefficient, and magnetoresistance of thin samples of intrinsic Ge have been studied. The data are analyzed using the theory of Petritz (3497 above). The results indicate that light holes play an important role in the transport process in the surface. There is a reduction of the mobility of surface electrons in qualitative agreement with the predictions of Schrieffer (2322 of 1955).
- 537.311.33:546.289:538.63 3528
Magnetoresistance Symmetry Relation in n -Germanium—C. Goldberg and W. E. Howard. (*Phys. Rev.*, vol. 110, pp. 1035–1039; June 1, 1958.) Careful measurement of the weak-field magnetoresistance coefficients of n -type Ge indicates that the magnetoresistance symmetry relation is obeyed for samples with carrier concentrations as high as $6 \times 10^{15} \text{ cm}^{-3}$. For a 3×10^{16} sample, the deviation, if any, is still quite small. For samples with larger concentrations there is definite evidence of some deviation.
- 537.311.33:546.289:538.63:535.376 3529
The Electromagnetoluminescence Effect in Germanium—M. Bernard and J. Loudette. (*Compt. Rend. Acad. Sci., Paris*, vol. 246, pp. 1177–1180; February 24, 1958.) The emission of infrared radiation by a sample of Ge placed in an electric field at right angles to a magnetic field is due to the recombination of electrons and holes. This has been studied experimentally.
- 537.311.33:546.289:541.135 3530
The Rectifying Effect of Germanium/Electrolyte Contacts—G. Déjardin, G. Mesnard and A. Dolce. (*Compt. Rend. Acad. Sci., Paris*, vol. 246, pp. 1016–1018; February 17, 1958.) Measurements have been made of the I/V characteristics of single-crystal n -type Ge in contact with a 0.1 N solution of HCl, using 12-volt pulses of duration several microseconds, with and without a superimposed polarizing voltage of about 1 volt.
- 537.311.33:546.289:621.314.63 3531
On the Backward Leakage Current in the Alloyed Germanium p - n Junction—M. Kikuchi. (*J. Phys. Soc. Japan*, vol. 13, pp. 350–362; April, 1958.) Experimental procedure and results are described for the observation of "creep" phenomena (i.e., variation of current with a fixed applied voltage). Creep is observed in the leakage current component and it is also found that, in some alloy-junction transistors, the creep in the emitter junction influences the characteristics of the collector junction. Some theoretical considerations are suggested which partially explain the experimental results.
- 537.311.33:546.57.24 3532
Electrical Properties of Ag₂Te—S. Miyatani. (*J. Phys. Soc. Japan*, vol. 13, pp. 341–350; April, 1958.) Measurements of electronic conductivity, Hall constant and thermoelectric power have been made, for varying ratios of Ag/Te, using a galvanic cell Ag/AgI/Ag₂Te/Pt. The EMF of the cell represents the position of the Fermi level relative to Ag-saturated Ag/Te.
- 537.311.33:546.682.86 3533
High-Electric-Field Effects in n -Indium Antimonide—M. Glicksman and M. C. Steele. (*Phys. Rev.*, vol. 110, pp. 1204–1205; June 1, 1958.) Pulsed current/voltage measurements have been made at 77°K on a single crystal of n -type InSb up to a current density of 10^4 a/cm^2 . Beyond about $2 \times 10^3 \text{ a/cm}^2$ the current increased rapidly for small further increases in voltage. The mechanism of electron-hole pair creation is used to explain the results. See also 2148 of 1958 (Prior).
- 537.311.33:546.682.86 3534
Theory of Cyclotron Resonance Absorption by Conduction Electrons in Indium Antimonide—R. F. Wallis. (*Phys. Chem. Solids*, vol. 4, nos. 1/2, pp. 101–110; 1958.) A semiclassical treatment, assuming a simple conduction band with a minimum at $k=0$, and neglecting spin interactions.
- 537.311.33:546.682.86 3535
Influence of Crystal Orientation on the Surface Behaviour of InSb—M. C. Lanine, A. J. Rosenberg and H. C. Gatos. (*J. Appl. Phys.*, vol. 29, pp. 1131–1132; July, 1958.)
- 537.311.33:[546.682.86+546.289]:535.33-1 3536
The Infrared Emissivities of Indium Antimonide and Germanium—T. S. Moss and T. D. H. Hawkins. (*Proc. Phys. Soc.*, vol. 72, pp. 270–273; August 1, 1958.)
- 537.311.33:546.682.86:538.63 3537
Magnetoresistance and Field Dependence of the Hall Effect in Indium Antimonide—G. Fischer and D. K. C. MacDonald. (*Canad. J. Phys.*, vol. 36, pp. 527–538; May, 1958.) Measurements of resistance and Hall effect show both to be highly dependent on magnetic field. The classical two-band model, often proposed to account for the behavior of metals, is found to account quite well for the observed results up to the highest fields used. The underlying assumptions of this theory are reviewed and simple formulas are derived, allowing the concentration and mobilities of both types of carrier to be calculated from the magnetic-field dependence of the resistivity and Hall effect.
- 537.311.33:621.314.63:537.52 3538
The Avalanche Breakdown Voltage of Narrow p^+n^+ Diodes—J. Shields. (*J. Electronics Control*, vol. 4, pp. 544–548; June, 1958.) Considerable reduction in breakdown voltage can occur when the width of the junction is reduced below a limiting value, the effect becoming more pronounced as the net impurity concentration in the v region is decreased. The breakdown voltage is much higher than the voltage at which penetration of the space-charge region occurs. See also 2152 of 1958.
- 537.311.33:621.315.61 3539
Simplified Theory of One-Carrier Currents with Field-Dependent Mobilities—M. A. Lampert. (*J. Appl. Phys.*, vol. 29, pp. 1082–1090; July, 1958.) A general method is presented for the calculation of steady-state, one-carrier currents in nonmetallic solids where the mobility is field-dependent. See also 832 of 1957.
- 537.312.62:534.23-8 3540
Ultrasonic Attenuation in Superconductors—H. E. Bömmel and W. P. Mason. (*Bell Lab. Rec.*, vol. 36, pp. 253–256; July, 1958.) Metals in the normal resistivity state give large attenuation for ultrasonic waves of sufficiently high frequency, but in the superconducting state the attenuation drops to zero as the temperature approaches 0°K. Results for lead and for very pure tin are given and the effect of an applied magnetic field is discussed.
- 538.22 3541
Magnetic Structures of MnO, FeO, CoO, and NiO—W. L. Roth. (*Phys. Rev.*, vol. 110, pp. 1333–1341; June 15, 1958.)
- 538.22:538.569.4 3542
Quantitative Theory of Faraday Rotation at Centimetre Wavelengths in Chrome Alum, and its Experimental Verification—B. C. Uhal, A. Chevalier, and T. Kahan. (*Compt. Rend. Acad. Sci., Paris*, vol. 246, pp. 901–903; February 10, 1958.) The theory is valid for the region of parametric transparency where the spin-spin interaction does not occur.

- 538.22:546.65/.66 3543
Magnetic Properties of the Gd-La and Gd-Y Alloys—W. C. Thoburn, S. Legvold, and F. H. Spedding. (*Phys. Rev.*, vol. 110, pp. 1298-1301; June 15, 1958.)
- 538.221 3544
Excitation of Spin Waves in a Ferromagnet by a Uniform R.F. Field—C. Kittel. (*Phys. Rev.*, vol. 110, pp. 1295-1297; June 15, 1958.) It is possible to excite exchange and magneto-static spin waves in a ferromagnet by a uniform RF field provided that spins on the surface of the specimen experience anisotropy interactions different from those acting on spins in the interior.
- 538.221 3545
Theory of the Curvature of Bloch Walls under the Influence of Stray Fields—H. D. Dietze. (*Z. Phys.*, vol. 149, pp. 276-298; October 19, 1957.) The influence of stray fields on the initial permeability is investigated with reference to Kersten's theory (see *e.g.*, 1825 of 1957).
- 538.221 3546
Experimental Investigation of the Kinetics of Magnetic Moments in Iron above the Curie Point—M. Ericson and B. Jacrot. (*Compt. Rend. Acad. Sci., Paris*, vol. 246, pp. 1018-1020; February 17, 1958.)
- 538.221:538.652 3547
Magnetostriction Curves of Polycrystalline Ferromagnetics—E. W. Lee. (*Proc. Phys. Soc.*, vol. 72, pp. 249-258; August 1, 1958.)
- 538.221:539.23 3548
Thin Ferromagnetic Layers. Electrical Properties of Thin Films of Nickel—G. Goureaux and A. Colombani. (*Compt. Rend. Acad. Sci., Paris*, vol. 246, pp. 741-744; February 3, 1958.)
- 538.221:621.318.122 3549
Hysteresis Loops associated with a Simple Domain Structure—A. Hart. (*Proc. Phys. Soc.*, vol. 72, pp. 244-248; August 1, 1958.)
- 538.221:621.318.124 3550
Origin of Magnetic Anisotropy in Cobalt-Substituted Magnetite—J. C. Slonczewski. (*Phys. Rev.*, vol. 110, pp. 1341-1348; June 15, 1958.)
- 538.221:621.318.12.029.65 3551
Magnetic Materials for Use at High Microwave Frequencies (50-90 kmc/s)—F. K. du Pré, D. J. De Bitetto, and F. G. Brockman. (*J. Appl. Phys.*, vol. 29, pp. 1127-1128; July, 1958.) Experimental results show that the no-field resonance line in oriented ferroxidure ($\text{BaO} \cdot 6\text{Fe}_2\text{O}_3$) can be placed at any frequency in the 50-90-km range by partial substitution of Fe_2O_3 by Al_2O_3 . Similar effects occur in $\text{SrO} \cdot 6\text{Fe}_2\text{O}_3$. See also Guillaud and Villers (3451 of 1956).
- 538.221:621.318.134 3552
Switching in Rectangular-Loop Ferrites containing Air Gaps—U. F. Gianola. (*J. Appl. Phys.*, vol. 29, pp. 1122-1124; July, 1958.) Switching waveforms produced by ferrite magnetic cores with or without air gaps are given and discussed with reference to predicted characteristics.
- 538.221:621.318.134 3553
Magnetization Processes in a Polycrystalline Manganese Zinc Ferrite—L. F. Bates, H. Clow, D. J. Craik, and P. M. Griffiths. (*Proc. Phys. Soc.*, vol. 72, pp. 224-232; August 1, 1958.) A description is given of Bitter-figure, magnetothermal and Barkhausen-effect studies which indicate that the processes of magnetization are entirely rotational.
- 538.221:621.318.134:538.569.4 3554
Ferromagnetic Resonance Line Width in Yttrium Iron Garnet Single Crystals—R. C. LeCraw, E. G. Spencer, and C. S. Porter. (*Phys. Rev.*, vol. 110, pp. 1311-1313; June 15, 1958.) Waveguide cavity perturbation techniques are used with samples of diameter 0.013-0.020 inch. An extremely narrow line width of 520 millioersteds (the full width) is observed at 9300 mc along the hard axis [100]. The approximate invariance of the line width with frequency is compared with theoretical predictions. See also 21569 of 1958.
- 538.221:621.318.134:621.372.8 3555
Investigation of the Dependence of Certain Properties of Ferrites on Temperature in the Centimetre-Wave Range—V. A. Kuseleva and E. I. Kondorskii. (*Dokl. Akad. Nauk S.S.S.R.*, vol. 119, pp. 926-928; April 11, 1958.) Experiments carried out on samples of $\text{Ni}_0.7\text{Mg}_{0.3}\text{Fe}_2\text{O}_4$ in circular and rectangular waveguides showed that with rise of temperature resonance occurs at reduced field strength. This seems to be related to the variation of the field anisotropy. The rotation of the plane of polarization due to a magnetic field for different temperatures, and the temperature dependence of the resonance field are shown. Ellipticity and attenuation ratios for temperatures between -196 and +220°C and different magnetic field strengths are tabulated.
- 549.514.51:537.228.1 3556
Elastic and Piezoelectric Constants of Alpha-Quartz—R. Bechmann. (*Phys. Rev.*, vol. 110, pp. 1060-1061; June 1, 1958.) Results obtained by the resonance method (2116 of 1958) are tabulated.
- 621.315.612:537.311.3 3557
The Effect of Temperature and Thickness on the Electrical Resistivity of Ceramic Coatings—W. H. Fischer. (*J. Electrochem. Soc.*, vol. 105, pp. 201-203; April, 1958.)
- MATHEMATICS
- 517.566:621.396.822 3558
The Axis-Crossing Intervals of Random Functions—J. A. McFadden. (*IRE TRANS. ON INFORMATION THEORY*, vol. IT-2, pp. 146-150; December, 1956. Abstract, *PROC. IRE*, vol. 45, p. 575; April, 1957.)
- 517.9:512.831 3559
Differential Equations, Difference Equations and Matrix Theory—P. D. Lax. (*Commun. Pure Appl. Math.*, vol. 11, pp. 175-194; May, 1958.) For comments by H. F. Weinberger see *ibid.*, pp. 195-196.
- 517.9:534.1 3560
On the Periodic Solutions of the Forced Oscillator Equation—R. M. Rosenberg. (*Quart. Appl. Math.*, vol. 15, pp. 341-354; January, 1958.)
- 519.2:621.391 3561
Some General Aspects of the Sampling Theorem—D. L. Jagerman and L. J. Fogel. (*IRE TRANS. ON INFORMATION THEORY*, vol. IT-2, pp. 139-146; December, 1956. Abstract, *PROC. IRE*, vol. 45, p. 575; April, 1957.)
- MEASUREMENTS AND TEST GEAR
- 529.78:621.374 3562
The Accurate Measurement of a Time Interval—A. E. Cawwell and H. Ristlaid. (*Electronic Eng.*, vol. 30, pp. 502-503; August, 1958.) A method is described for measuring the time interval between trigger pulse and output pulse in a delay unit. Measurements accurate to within ± 0.02 per cent can be made of a time interval in the ms range.
- 529.786:621.317.7.087.6 3563
A System for the Electrical Recording of Time Intervals—G. Becker. (*Elektrotech. Z., Ed. A*, vol. 79, pp. 358-361; May 11, 1958.) Equipment is described for the continuous comparison of the frequencies of two quartz clocks. A mechanism similar to a synchronous stopwatch, and a magnetic counting system are used to derive a recorder voltage proportional to the time interval being measured.
- 53.087.64 3564
Automatic Calibrator for Chart Recorders—J. L. Durand. (*Rev. Sci. Instr.*, vol. 29, pp. 534-535; June, 1958.) A circuit is outlined which produces calibration pips on a magnetic-resonance spectrometer chart.
- 621.3.018.41(083.74):621.396.712 3565
WWV Standard-Frequency Transmissions—W. D. George. (*Proc. IRE*, vol. 46, pp. 1534-1535; August, 1958.) A note on the accuracy of WWV and WWVH transmissions during May, 1958.
- 621.3.082+621.3.078 3566
How Transducers Measure and Control—R. K. Jurgen. (*Electronics*, vol. 31, pp. 59-70; July 4, 1958.) A general survey of the transducer field, together with applications.
- 621.317.332.6.029.6 3567
Measurement of Low Reflection Coefficients at High Frequencies in Terms of Magnitude and Phase—A. Linnebach. (*Arch. Elekt. Übertragung*, vol. 11, pp. 471-477; December, 1957.) The conventional reflectometer method is extended to cover the measurement of phase angle by the insertion of a quadripole with variable stub lines.
- 621.317.35:621.396.84 3568
Errors of Selectivity Measurement—W. Rotkiewicz. (*Nachricht. Z.*, vol. 8, pp. 22-24; January, 1958.) The causes of errors and their elimination in receiver selectivity measurements are discussed.
- 621.317.411.029.6:538.221 3569
Measurement of Permeability at V.H.F. using Transmission-Line Technique—J. C. Anderson. (*J. Brit. IRE*, vol. 18, pp. 417-424; July, 1958.) Accurate measurements may be made without the aid of calibrated instruments or standing-wave detectors. These measurements are sufficiently precise to show detailed structure in the permeability/frequency curves. Results are given for strips of permalloy B and C, mumetal, and for pure nickel wire.
- 621.317.42:621.375.13 3570
The Control of Flux Waveforms in Iron Testing by the Application of Feedback Amplifier Techniques—J. McFarlane and M. J. Harris. (*Proc. IEE*, vol. 105, pp. 395-402; Discussion, pp. 402-405; August, 1958.)
- 621.317.42:621.383 3571
The Construction of a Photoelectric Electronic Fluxmeter—M. Sauzade. (*Compt. Rend. Acad. Sci., Paris*, vol. 246, pp. 727-730; February 3, 1958.) Description of the design of an integrating system comprising a galvanometer, photocell and amplifier, with capacitive feedback, of the type described by Edgar [see 2163 of 1956 (Kapitsa)]. See also 435 of 1949 (Dicke).
- 621.317.44 3572
A Ferrometer for the Determination of the A.C. Magnetization Curve and the Iron Losses of Small Ferromagnetic Sheet Samples—H. Blomberg and P. J. Karttunen. (*Proc. IEE*, vol. 105, pp. 375-384; August, 1958. Discussion, pp. 402-405.)
- 621.317.44 3573
Direct-Reading Iron-Loss Testing Equip-

ment for Single Sheets, Single Strips and Test Squares—J. McFarlane, P. Milne, and J. K. Darby. (*Proc. IEE*, vol. 105, pp. 385-394; August, 1958. Discussion, pp. 402-405.)

621.317.7:538.566:621.372.823 3574
Double-Probe Polarimetric Analyser for the 1000-mc/s Band—F. Picherit. (*Compt. Rend. Acad. Sci., Paris*, vol. 246, pp. 911-913; February 10, 1958.) Description of apparatus for accurate measurement of wave rotation in a circular waveguide, using a graduated rotatable section provided with two probes with a fixed angular separation of 90 degrees.

621.317.73:537.312.9.082.73 3575
Apparatus for Piezoresistance Measurement—M. Pollack. (*Rev. Sci. Instr.*, vol. 29, pp. 639-641; July, 1958.) The piezoresistance effect in semiconductors is measured using a 29-cps alternating stress. The method is sensitive and suitable for low-resistivity materials; the measurements are adiabatic. See also 1192 of 1958 (Potter).

621.317.733:621.317.4:538.221 3576
Improved Bridge Method for the Measurement of Core Losses in Ferromagnetic Materials at High Flux Densities—W. P. Harris and I. L. Cooter. (*J. Res. Natl. Bur. Stand.*, vol. 60, Rep. 2865, pp. 509-516; May, 1958.) An amplifier having negative output resistance was devised and is used in a manner that automatically allows accurate compensation for the harmonic components of the excitation current. See also 530 of 1957 (Cooter and Harris).

621.317.74:621.372.2.029.6 3577
High-Frequency Measuring Lines—C. Moerder. (*Arch. Tech. Messen.*, no. 265, pp. 37-40; February, 1958.) The use of calibrated transmission lines for the measurement of circuit and line characteristics is described. Particular reference is made to the Smith chart and to commercial test equipment incorporating an artificial line with a CRO display of the measured parameters on a Smith-chart graticule.

621.317.74:621.372.852.323:621.318.134 3578
High-Power Testing of Ferrite Isolators—E. Wantuch. (*Electronic Ind.*, vol. 17, pp. 83-85; April, 1958.) Description of methods for determining insertion loss, input SWR under matched-load, and isolation under mismatched-load conditions.

621.317.74:621.374 3579
An Electronic Pulse-Duration Analyser—E. Newell and A. A. Makemson. (*P.O. Elec. Eng. J.*, vol. 51, pp. 64-69; April, 1958.) Description of apparatus for determining the duration and frequency of occurrence of transient irregularities on HF trunk telephone routes. Irregularities longer than 2 ms are recorded on cold-cathode counters, simultaneous recordings being made of durations exceeding four predetermined values in the range 2-50 ms.

621.317.75:621.376.3 3580
Testing the Linearity of Modulators and Demodulators in Multichannel F.M. Transmitters and Receivers—G. C. Davey. (*Electronic Eng.*, vol. 30, pp. 487-489; August, 1958.) Design principles are described of equipment which displays the slope of a demodulator characteristic and discriminates changes in slope of 1 per cent. Modulators can be tested indirectly and the equipment may be used for conventional sweep tests in aligning IF amplifiers.

621.317.755 3581
A New Eight-Channel Oscillograph—H. H. Feldmann. (*Elektrotech. Z.*, Ed. B, vol. 10, pp. 206-209; May 21, 1958.) A single-tube CRO is described which provides facilities for the

simultaneous display of four functions. The 2×4 variables are applied to the vertical and horizontal amplifiers, via an electronic switching circuit.

621.317.755:621.385.029.6 3582
Fractional-Millimicrosecond Oscilloscope System Utilizing Commercially Available Components—C. N. Winningstad. (*Rev. Sci. Instr.*, vol. 29, pp. 578-584; July, 1958.) The oscilloscope described uses a traveling-wave CR tube with a synchronizing system which does not appreciably distort the applied pulse.

621.317.755.087.6 3583
Electronic Tracing of Oscilloscope Displays—C. H. Hertz and E. Möller. (*Rev. Sci. Instr.*, vol. 29, pp. 611-613; July, 1958.) A gated charging circuit is described for sampling the waveform applied to a CRO and driving a pen recorder. Frequencies up to 10 kc can be recorded.

621.317.789 3584
Ergometer measures Bursts of Energy—L. A. Rosenthal. (*Electronics*, vol. 31, pp. 79-81; June 6, 1958.) Energy surges unbalance a bolometer bridge whose output is amplified and applied to a peak-holding voltmeter; the instrument is calibrated by using an internally generated pulse of known energy content.

621.317.799:551.510.535:621.396.11 3585
An Automatic Recorder for Measuring Ionospheric Absorption—Mazumdar. (See 3461.)

621.317.799:621.316.82 3586
Potentiometer Tester—S. Morleigh. (*Wireless World*, vol. 64, pp. 450-452; September, 1958.) Description of circuits for locating bad contacts and for measuring contact resistance in precision variable resistors and inductive potentiometers.

621.317.799:621.396.61/.62 3587
Recent Developments in Communications Measuring Instruments—E. Garthwaite and A. G. Wray. (*J. Brit. IRE*, vol. 18, pp. 387-397; July, 1958.) Improvements in design and advances in measuring techniques are illustrated by reference to specific instruments. Future trends are briefly discussed.

621.317.799:621.396.933.029.6 3588
A Standing-Wave-Ratio Measuring Instrument for Use in the Maintenance of Aircraft Installations—A. G. Hancock and T. S. Kepner. (*A.W.A. Tech. Rev.*, vol. 10, pp. 90-99; October, 1957.) A portable instrument for measuring SWR on transmission lines in VHF aircraft installations is described. The battery operated equipment includes bridges for 50-Ω and 70-Ω installations, and fixed and variable oscillators.

OTHER APPLICATIONS OF RADIO AND ELECTRONICS

53.087.5 3589
Digital and Pictorial Photographic Electronic Recorder—R. G. McPherson and I. A. Sonderby. (*Commun. and Electronics*, no. 36, pp. 194-196; May, 1958.) Digital recording is achieved by photographing square spots or bits in rows on the film. With a bit size of 10 mils and 40 bits/row, 4000 bits/inch may be stored on 16-mm film. Playback is effected by mechanical or electrical scanning.

53.087.9:621.395.625.3 3590
Magnetic Tape for Data Recording—C. D. Mee. (*Proc. IEE*, vol. 105, pp. 373-380; July, 1958. Discussion, pp. 380-382.) The occurrence of "drop-outs" in both the recording and reproduction of pulse signals is investigated and applied to "return to zero" and "non return to

zero" recording. Methods are considered which would improve reliability. Equipment is described for testing tape under widely varying recording conditions. Commercial tapes are assessed and an economical performance specification is suggested.

551.508.822 3591
Comparison of Aerological Soundings made Simultaneously by Radiosonde and Aircraft—F. H. Ludlam and P. M. Saunders. (*Tellus*, vol. 10, pp. 83-87; February, 1958.) The results of five soundings by Väisälä radiosonde and by aircraft fitted with electrical resistance thermometers show that the temperatures given by the radiosonde were usually 1-1½°C, but occasionally 2½-3½°C, too great. Shallow layers of very dry air were often not revealed by the radiosonde due to the large time lag of the hygrometer unit.

621.362:536.8 3592
Measured Thermal Efficiencies of a Diode Configuration of a Thermo-electron Engine—G. N. Hatsopoulos and J. Kaye. (*J. Appl. Phys.*, vol. 29, pp. 1124-1125; July, 1958.) Note on a practical engineering method of converting heat directly into electricity.

621.384.612 3593
Electron Losses due to Phase Oscillations Induced by Radiation Fluctuations in Synchrotrons—A. N. Matveev. (*Zh. Eksp. Teor. Fiz.*, vol. 33, pp. 1254-1260; November, 1957.) An approximate method of calculation is described taking account of nonlinear effects by considering appropriate boundary conditions in linear theory.

621.384.7:537.533.8 3594
Source of Ions due to Electron Bombardment—D. Blanc and A. Degeilh. (*Compt. Rend. Acad. Sci., Paris*, vol. 246, pp. 936-939; February 10, 1958.) The characteristics of an ion source of Nier type (see *Rev. Sci. Instr.*, vol. 18, pp. 398-411; June, 1957) without an auxiliary magnetic field are described.

621.385.833:061.3 3595
Summarized Proceedings of a Conference on Electron Microscopy—Bangor, September 1957—H. W. Emerton. (*Brit. J. Appl. Phys.*, vol. 9, pp. 306-312, 322; August, 1958.)

621.385.833:537.533.72 3596
Magnetic Deflexion of Electron Beams without Astigmatism—G. D. Archard and T. Mulvey. (*J. Sci. Instr.*, vol. 35, pp. 279-283; August, 1958.) The system described uses circular pole pieces from which semicircular portions have been removed. An application to reflection-type electron microscopes is described.

621.385.833:621.373.44 3597
Construction of a 100-kV Pulse Generator—J. Gardez. (*Compt. Rend. Acad. Sci., Paris*, vol. 246, pp. 1023-1025; February 17, 1958.) A pulse generator for an electron microscope is described, with pulse length 2 μsec, and repetition frequency 200/sec.

621.387.4 3598
The Design, Performance and Use of Fission Counters—W. Abson, P. G. Salmon, and S. Pyrah. (*Proc. IEE*, vol. 105, pp. 349-356; July, 1958. Discussion, pp. 365-369.) General design criteria applicable to the measurement of fission cross sections, the analysis of neutron spectra and the relative measurement of neutron flux are discussed.

621.387.424 3599
Firing Characteristics of Halogen-Quenched Geiger-Müller Counters—S. P. Puri and P. S. Gill. (*Proc. Natl. Inst. Sci. India*, vol. 24, pp. 66-77; January 26, 1958.)

621.387.426.2 3600

Boron Trifluoride Proportional Counters—W. Abson, P. G. Salmon, and S. Pyrah. (*Proc. IEE*, vol. 105, pp. 357–365; July, 1958. Discussion, pp. 365–369.) Operating characteristics and the effect of circuit parameters on output pulse amplitude are discussed.

621.398:623.454.91–519 3601

Telemeter Transmitter for Vanguard Rocket—N. Raskhodoff. (*Electronics*, vol. 31, pp. 46–47; July 4, 1958.) Details of engine performance are relayed using a PWM/FM system.

PROPAGATION OF WAVES

621.396.11:551.510.535 3602

Electromagnetic Propagation in an almost Homogeneous Medium—V. W. Bolie. (*Aust. J. Phys.*, vol. 2, pp. 118–125; March, 1958.) An equation is derived for calculating the scattering energy resulting from a single Gaussian perturbation in refractive index. A turbulent ionosphere may be considered as being composed of such perturbations.

621.396.11:551.510.535 3603

Single-Hop Propagation of Radio Waves to a Distance of 5300 km—F. Kift. (*Nature, London*, vol. 181, pp. 1459–1460; May 24, 1958.) Path lengths and angles of elevation of rays arriving at Slough from Ottawa have been calculated from the Appleton and Beynon equations for propagation via a parabolic F_2 layer, and show good agreement with experimental results of Warren and Hagg (2202 of 1958).

621.396.11.029.45/.5:551.510.535 3604

Low-Frequency Reflection in the Ionosphere—H. Poeverlein. (*J. Atmos. Terr. Phys.*, vol. 12, nos. 3/4, pp. 126–139; 1958 and no. 4, pp. 236–247; 1958. Correction, *ibid.*, p. 352.) Theoretical investigation of ionospheric reflection in the frequency range 1–100 kc approximately. The ionospheric layer is considered as a thin conductive sheet or as consisting of many thin sublayers. Some typical cases are discussed with reference to observational results.

621.396.11.029.45:551.594.6 3605

Velocity of Propagation of Electromagnetic Waves at Audio Frequencies—Y. L. Al'pert and S. V. Borodina. (*Zh. Eksp. Teor. Fiz.*, vol. 33, pp. 1305–1307; November, 1957.) Note of an investigation covering the frequency range 1–30 kc based on waveform analysis of thunderstorm discharges at distances of 800–3100 km. Experimental and theoretical values deviate significantly below 3 kc, at which frequencies the model of the ionosphere used in the calculations may be inappropriate. See also 920 of 1957.

621.396.11.029.53:551.510.535 3606

Investigation of Magneto-ionic Fading in Oblique-Incidence Medium-Wave Transmissions—M. S. Rao and B. R. Rao. (*J. Atmos. Terr. Phys.*, vol. 12, pp. 293–305; July, 1958.) "Periodic fading of magneto-ionic origin observed in oblique-incidence medium-wave records is interpreted theoretically by calculating the phase paths by a graphical integration method assuming Chapman and parabolic ion distribution. Analytical expressions have also been derived for phase paths of both magneto-ionic components by an approximate method involving the use of an empirical formula for q - x curves. The theoretical values of fading periods compared very well with the experimental data, the agreement being particularly good for the case of Chapman distribution."

621.396.11.029.6:551.510.5 3607

Atmospheric Effects on V.H.F. and U.H.F. Propagation—G. H. Millman. (*Proc. IRE*, vol.

46, pp. 1492–1501; August, 1958.) Tropospheric refractive-index profiles and ionospheric electron-density models representative of average conditions are presented, and mathematical relations are derived for calculating refraction effects, time delays, Doppler errors, polarization changes, and attenuation experienced by radio waves traversing the entire atmosphere.

621.396.11.029.62:523.5 3608

A Theoretical Rate Amplitude Relation in Meteoric Forward Scatter—C. O. Hines. (*Canad. J. Phys.*, vol. 36, pp. 539–554; May, 1958.) The theory of forward scattering of radio waves by ionized meteor trails is applied to the development of a relation which expresses the expected occurrence rate of scattered signals exceeding a given amplitude level as a function of that level. Comparison with provisional observational data shows good agreement qualitatively and quantitatively. Closest agreement is obtained only with an appropriate choice of two scaling factors which provide a convenient condensed version of the observations for further interpretation.

621.396.11.029.62:523.5 3609

Observations of Angle of Arrival of Meteor Echoes in V.H.F. Forward-Scatter Propagation—K. Endresen, T. Hagfors, B. Landmark and J. Rodsrud. (*J. Atmos. Terr. Phys.*, vol. 12, pp. 329–334; July, 1958.) Observations were made in November and December, 1957 near Tronsö, using a frequency of 46.8 mc. Histograms show the properties of background meteor reflections as well as of shower reflections as a function of azimuth. Diurnal variations agree well with present theories.

621.396.11.029.62:523.5 3610

The Fading of Long-Duration Meteor Bursts in Forward-Scatter Propagation—B. Landmark. (*J. Atmos. Terr. Phys.*, vol. 12, pp. 341–342; July, 1958.) Application of the theory presented by L. A. Manning at the 12th General Assembly of URSI, 1957, Boulder, Colo., allows the seasonal variations of wind shear in the lower E layer to be studied.

621.396.11.029.62:551.510.535 3611

Preliminary Results of Studies of the Angular Distribution of a V.H.F. Ionospheric Forward-Scatter Signal—T. Hagfors. (*J. Atmos. Terr. Phys.*, vol. 12, pp. 340–341, plate; July, 1958.) The angular spectrum is determined by correlation over the wavefront. Results obtained at 46.8 mc over a 1150-km N-S path indicate that the Rayleigh-type background is not due to the overlapping of many small meteoric echoes.

621.396.11.029.62:621.397.81 3612

Phase-Coherent Back-Scatter of Radio Waves at the Surface of the Sea—E. Sofaer. (*Proc. IRE*, vol. 105, pp. 383–394; July, 1958.) An investigation into interference with reception of the B.B.C. Devon television transmitter in coastal regions near Plymouth. Rhythmic variations in amplitude due to beating between direct and back-scattered signals occur when sea waves within the irradiated area are correctly spaced and suitably oriented with respect to frequency and geometry of the transmitter/receiver circuit. The effect is studied theoretically and correlated with meteorological data.

621.396.11.029.64 3613

Multipath Propagation of Microwaves—T. Omori and R. Sato. (*Rep. Elec. Commun. Lab., Japan*, vol. 6, pp. 1–11; January, 1958.) Results are given for five different paths at frequencies near 4 kmc; frequency-sweep and pulse techniques were both used to measure the delayed signals. The mean value of the instantaneous distortion in the worst 1-hour period was shown to be negligibly small.

RECEPTION

621.376.2 3614

The Demodulation of Linearly Distorted A.M. Spectra—H. Schneider and G. Petrich. (*Nachricht. Z.*, vol. 8, pp. 17–21; January, 1958.) Continuation of 2893 of 1957 dealing with s.s.b. and common-frequency reception and the distortion effects of overmodulation.

621.376.23:621.396.822 3615

The Rectification of Non-Gaussian Noise—J. A. Mullen and D. Middleton. (*Quart. Appl. Math.*, vol. 15, pp. 395–419; January, 1958.) A noise model in which the noise events occur with a Poisson distribution in time is analyzed. Atmospheric and some types of radar clutter may approximate to this model. The influence of linear and quadratic detectors on the noise is studied, and account is taken of narrow-band filters preceding the detector.

621.376.23:621.396.822 3616

Effects of Signal Fluctuation on the Detection of Pulse Signals in Noise—M. Schwartz. (*IRE TRANS. ON INFORMATION THEORY*, vol. IT-2, pp. 66–71; June, 1956. Abstract, *Proc. IRE*, vol. 44, p. 1642; November, 1956.)

621.396.822:621.376.23 3617

Rectification of Two Signals in Random Noise—L. L. Campbell. (*IRE TRANS. ON INFORMATION THEORY*, vol. IT-2, pp. 119–124; December, 1956. Abstract, *Proc. IRE*, vol. 45, p. 575; April, 1957.)

621.376.23:621.396.822 3618

Optimum Detection of Random Signals in Noise, with Applications to Scatter-Multipath Communication: Part I—R. Price. (*IRE TRANS. ON INFORMATION THEORY*, vol. IT-2, pp. 125–135; December, 1956. Correction, *ibid.*, vol. IT-3, p. 256; December, 1957. Abstract, *Proc. IRE*, vol. 45, p. 575; April, 1957.)

621.376.23:621.396.822 3619

A Coincidence Procedure for Signal Detection—M. Schwartz. (*IRE TRANS. ON INFORMATION THEORY*, vol. IT-2, pp. 135–139; December, 1956. Abstract, *Proc. IRE*, vol. 45, p. 575; April, 1957.)

621.376.332:621.3.018.78 3620

Amplitude Modulation Suppression in F.M. Systems—C. L. Ruthroff. (*Bell Sys. Tech. J.*, vol. 37, pp. 1023–1046; July, 1958.) Limiter circuits are analyzed in terms of low-index modulation theory. The analysis of a diode limiter shows that perfect AM suppression is possible with only small loss to the FM signal. Experimental verification is given.

621.396.62:621.396.662 3621

A Novel Sideband Selector System—E. P. Alvernaz. (*QST*, vol. 42, pp. 18–20; May, 1958.) Two mixers and a common VFO are used in a selector system by means of which an incoming signal, or any part of it, can be placed in or out of the pass band of a fixed-frequency band-pass filter without changing the receiver tuning.

621.396.662 3622

Some Aspects of Permeability Tuning—W. D. Meewezen. (*Proc. IRE, Aust.*, vol. 18, pp. 263–275; August, 1957.) Capacitance and permeability-tuned circuits are compared, and the construction and applications of permeability tuners are described.

621.396.8:519.2 3623

Cumulative Frequency Curves of Eccentric Rayleigh Distribution and their Application to Propagation Measurements—H. Zuhrt. (*Arch. elekt. Übertragung*, vol. 11, pp. 478–484; December, 1957.) Equations and curves of eccentric Rayleigh distribution are given which are

applicable to received voltage waveforms considered as a number of statistically fluctuating interference waves superimposed on the signal waveform. Probability distribution curves based on propagation measurements at 2.5, 4.15 and 15 kmc are compared with the theoretical curves; agreement is closed except for short-term probabilities.

621.396.82 3624
Radio Interference: Part 3—Suppression—
 R. A. Dilworth. (*P.O. Elec. Eng. J.*, vol. 51, pp. 40-45; April, 1958.) Interference produced by sparking from electrical appliances is discussed. Reduction of interference by measures taken at the receiving installation, and by suppression at source are considered. Practical suppression arrangements are described and illustrated for various kinds of appliance. Part 2: 2213 of 1958 (Britton).

621.396.821 3625
Atmospheric Noise Interference to Medium-Wave Broadcasting—
 S. V. C. Aiyar. (*Proc. IRE*, vol. 46, pp. 1502-1509; August, 1958.) The electrical discharges associated with a tropical thundercloud are described. It is suggested that discharge mechanisms within the cloud contribute noise only on frequencies above 2.5 mc. The power radiated by a flash in the medium-wave band is deduced by assuming that the energy is produced by the first stepped leader propagated as an air or ground discharge. See also 1866 of 1958.

STATIONS AND COMMUNICATION SYSTEMS

621.391 3626
Bits of Information—
 A. S. Zamanakos. (*Commun. and Electronics*, no. 36, pp. 197-201; May, 1958.) Concepts of information, channel capacity and equivocation are reviewed. The probability of an error is used to calculate the equivocation. The method of coding a message to incorporate error detecting and correcting information is explained, and examples are given of a parity checking procedure.

621.391 3627
On the Shannon Theory of Information Transmission in the Case of Continuous Signals—
 A. N. Kolmogorov. (*IRE TRANS. ON INFORMATION THEORY*, vol. IT-2, pp. 102-108; December, 1956.)

621.391 3628
On Noise Stability of a System with Error-Correcting Codes—
 V. I. Siforov. (*IRE TRANS. ON INFORMATION THEORY*, vol. IT-2, pp. 109-115; December, 1956. Abstract, *Proc. IRE*, vol. 45, p. 575; April, 1957.)

621.391 3629
Optimum, Linear, Discrete Filtering of Signals containing a Nonrandom Component—
 K. R. Johnson. (*IRE TRANS. ON INFORMATION THEORY*, vol. IT-2, pp. 49-55; June, 1956. Abstract, *Proc. IRE*, vol. 44, p. 1642; November, 1956.)

621.391:519.272 3630
Correlation Electronics—
 F. H. Lange. (*Nachricht. Z.*, vol. 8, pp. 3-11; January, 1958.) The principles and purpose of correlation analysis are outlined with examples of applications in communications and electroacoustics.

621.391:519.272 3631
Simple Methods of Correlation Measurements—
 R. Fey. (*Nachricht. Z.*, vol. 8, pp. 12-16; January, 1958.) The analytical bases of four methods of determining autocorrelation functions are discussed, with an outline of appropriate measurement techniques.

621.391:534.75 3632
Information Transmission with Elementary Auditory Displays—
 Sumby, Chambliss, and Pollack. (See 3314.)

621.391:534.75 3633
Confidence Ratings and Message Reception for Filtered Speech—
 Decker and Pollack. (See 3315.)

621.391:621.396.822 3634
Probability Densities of the Smoothed "Random Telegraph Signal"—
 W. M. Wonham and A. T. Fuller. (*J. Electronics Control*, vol. 4, pp. 567-576; June, 1958.) The probability distribution of the output from a simple RC smoothing network is found when the input is a sequence of random square waves generated by a Poisson process. Results suggest a convenient experimental method for generating LF noise with Gaussian, rectangular, parabolic or elliptical probability density functions.

621.391:621.396.822 3635
Nonstationary Velocity Estimation—
 T. M. Burford. (*Bell Sys. Tech. J.*, vol. 37, pp. 1009-1021; July, 1958.) A nonstationary noise is approximated by the product of a stationary noise and a deterministic function of time. From observations of the sum of such a nonstationary noise and a linear signal, an estimate of the rate of change of the signal is obtained.

621.396.4:551.510.52 3636
White Alice—A New Radio Voice for Alaskan Outposts—
 W. H. Tidd. (*Bell Lab. Rec.*, vol. 36, pp. 278-283; August, 1958.) A tropospheric-scatter system is described for multi-channel telephone and telegraph communication between points 100-200 miles apart. 10-kw transmitters and 60-foot parabolic antennas are used at frequencies in the 750-950 mc band.

621.396.41 3637
Compressed Time boosts Single-Sideband Capacity—
 M. I. Jacob and J. Mattern. (*Electronics*, vol. 31, pp. 52-55; July 4, 1958.) Description of a time-sharing multiplex system which needs only one RF channel, with a single transmitter and receiver at each station. Received information is stored, and then expended and read-out between transmissions.

621.396.41:621.396.65 3638
The Simultaneous Transmission of Television and Telephone Multiplex over a Single Microwave Channel on the Trans-Canada TD-2 System—
 H. E. Curtis, V. C. P. Strahlendorf, and A. J. Wade. (*Commun. and Electronics*, no. 36, pp. 185-190; May, 1958.) Transmission considerations, terminal circuits and tests are discussed for a system simultaneously transmitting a television signal and a maximum of 180 telephone channels.

621.396.61/:62:535-14 3639
500-Million-Mc/s Transceiver—
 H. Pallatz. (*Radio-Electronics*, vol. 28, pp. 93-94; October, 1957.) Simple voice-communication equipment using a caesium-vapour lamp as transmitter is described.

621.396.932 3640
The Development of Radio Services for Coastal Traffic, Inland Waterways and Harbours—
 J. Mohrmann. (*Telefunken Ztg.*, vol. 30, pp. 225-232; December, 1957. English summary, p. 286.) The development of R/T services for ship-to-shore communication in Germany is outlined and details of some modern installations, including VHF services, are given.

SUBSIDIARY APPARATUS

621.316.5.004.6 3641
Physical Processes in Contact Erosion—
 L. H. Germer. (*J. Appl. Phys.*, vol. 29, pp.

1067-1082; July, 1958.) A general survey of erosion effects for relatively low voltages and currents.

621.316.721/:722:621.314.7 3642
Transistor Voltage and Current Stabilizers—
 E. Cassagnol and G. Giralt. (*Compt. Rend. Acad. Sci., Paris*, vol. 246, pp. 1020-1023; February 17, 1958.) Details are given of a current generator and a voltage generator using transistors and a Zener diode. Coupled together, the circuits provide a stabilized current supply of up to 300 ma.

621.316.93:621.314.63 3643
Electrical Protection for Transistorized Equipment—
 J. W. Phelps. (*Bell Lab. Rec.*, vol. 36, pp. 247-249; July, 1958.) Semiconductor diodes are used to limit excessive voltages accidentally placed on telephone circuits.

621.353/:355 3644
New Batteries for the Space Age—
 D. Linden and A. F. Daniel. (*Electronics*, vol. 31, pp. 59-65; July 18, 1958.) A survey of short-life electrochemical batteries, developed for extreme reliability at high discharge rates under stringent operating conditions. The main characteristics of recent types are given in tabulated form.

TELEVISION AND PHOTOTELEGRAPHY

621.397.5 3645
567 Lines—
 P. T. Weston. (*Wireless World*, vol. 64, pp. 442-443; September, 1958.) An alternative to the British 405-line television system is suggested in which a greater number of lines is achieved with a minimum of equipment changes.

621.397.5:535.623 3646
A Method for Controlling the Gray-Scale Equivalent of Colours used in Live and Filmed Television Scenic and Graphic Art—
 W. J. Wagner. (*J. Soc. Mot. Pict. Telev. Eng.*, vol. 67, pp. 369-373; June, 1958. Discussion.) Greys are graded in a scale of 20 steps from white to black, and the equivalence of colors presented on a monochromatic screen is based on this scale.

621.397.6.029.63 3647
A UHF Television Link for Outside Broadcasts—
 K. C. Quinton. (*B.B.C. Eng. Div. Monographs*, no. 19, pp. 1-20; June, 1958.) The merits of FM and AM systems are considered, and preliminary comparison tests over a short link with a mobile transmitter at 190 and 511 mc indicated FM to be preferable. A mobile transmitter delivering 17 watts at about 630 mc with 6-mc deviation to either a Yagi or corner-reflector antenna is described. Receiver IF is either 30 or 60 ms, with a noise factor of 14 db. Multipath distortion is still troublesome over such links, and possible means of reducing it are suggested.

621.397.611 3648
Improved Television Standards Converter—
 T. Worswick. (*Wireless World*, vol. 64, pp. 443-444; September, 1958.) For the B.B.C. Eurovision converter system an improvement of 10 db in signal/noise ratio has been achieved by using a 4½-inch image orthicon tube Type P812 in place of a 3-inch Type P807.

621.397.611:535.623 3649
A Flying-Spot Film Scanner for Colour Television—
 H. E. Holman, G. C. Newton, and S. F. Quinn. (*Proc. IEE*, vol. 105, pp. 317-328; July, 1958. Discussion pp. 329-330.) Film moving with uniform velocity is scanned by a series of displaced rasters in such a sequence that the system is applicable to 50 or 60-pps conditions. Three photomultipliers provide color analysis of the image, element by element, and directly

produce a video-frequency signal. A particular equipment is described.

621.397.611.2 3650

A French Portable TV Camera—J. Polonsky. (*J. Telev. Soc.*, vol. 8, pp. 423-431; April/June, 1958.) Technical requirements and design considerations are described for the Type-CP103 equipment weighing about 29 pounds and based on a vidicon camera tube. Transistors are used in the power supply circuits and synchronizing generator.

621.397.62 3651

Ultrasonic Tones Select TV Channels—N. Frihart and J. Krakora. (*Electronics*, vol. 31, pp. 68-69; June 6, 1958.) Television receiver tuning and power supply are remotely controlled by means of an ultrasonic magnetostriction transducer with transistor oscillator transmitting via an air path to a microphone in the receiver. See also 3669 of 1957 (Adler, *et al.*).

TRANSMISSION

621.376.222 3652

Some Aspects of High-Level Modulation—A. H. Koster. (*R.S.G.B. Bull.*, vol. 33, pp. 552-556; June, 1958.) The effects of speech compression on the output of a typical transmitter, together with circuits for reducing the resulting distortion, are described.

621.396.61:621.396.967 3653

The Frequency Stability of Self-Excited Transmitters Connected to a Load with Variable Phase—H. Schwindling. (*Telefunken Ztg.*, vol. 30, pp. 246-250; December, 1957. English summary, pp. 287-288.) The Rieke-diagram method is used to investigate the "long-line" effect with reference to rotating radar antennas.

TUBES AND THERMIONICS

621.314.63+621.314.7 3654

Crystal Valves—T. R. Scott. (*J. Telev. Soc.*, vol. 8, pp. 401-412; April/June, 1958.) The development of the crystal tube is reviewed with

particular reference to economic aspects. The likely future relation between the economics of crystal and thermionic tubes is discussed and the role of the former in various fields of electronic application is examined. The difficulties and advantages of the manufacture and use of crystal tubes is also discussed.

621.314.63:621.372.652 3655

Shot Noise in p - n -Junction Frequency Converters—A. Uhler, Jr. (*Bell Sys. Tech. J.*, vol. 37, pp. 951-988; July, 1958.) General equations for the noise figure of a p - n -junction diode with arbitrary minority-carrier storage are derived, and it is shown that a junction with purely capacitive nonlinear admittance, in theory, permits noiseless amplification. Nonlinear-resistance diodes can give low-noise frequency conversion with pulsed local-oscillator current, but cannot amplify. See also 3897 of 1956.

621.314.63:621.372.632 3656

Gain and Noise Figure of a Variable-Capacitance Up-Converter—D. Leenov. (*Bell Sys. Tech. J.*, vol. 37, pp. 989-1008; July, 1958.) The upper-sideband frequency conversion performance of a p - n -junction nonlinear-capacitance diode is analyzed. The maximum available gain and the noise figure are derived for the equivalent circuit consisting of a time-varying capacitance and constant series resistance. Over-all noise figures are given for three types of receiver with diode preamplifiers.

621.314.7 3657

The Tecnetron—Competitor to the Transistor?—E. Aisberg. (*Radio-Electronics*, vol. 29, pp. 60-61; May, 1958.) Description of a semiconductor device invented by S. Teszner (see *e.g.*, 3599 of 1954). It consists of a small rod of n -type Ge 0.5 mm in diameter with a central portion reduced to 30μ and surrounded by a cylinder of indium. Transconductance increases with frequency and in experiments a gain of 16 db was obtained at 200 mc. See also *Toute la Radio*, vol. 25, pp. 47-48; February, 1958, and *Wireless World*, vol. 64, p. 132; March, 1958.

621.385+621.375].029.65 3658

The Generation and Amplification of Millimetre Waves—Kleen and Pöschl. (See 3384.)

621.385.4:621.384.622 3659

The Resnatron as a 200-Mc/s Power Amplifier—E. B. Tucker, H. J. Schulte, E. A. Day, and E. E. Lampi. (*Proc. IRE*, vol. 46, pp. 1483-1492; August, 1958.) A description of the tubes used in the Minnesota linear proton accelerator. They are continuously pumped grid-pulsed amplifiers with a peak power output of 3.5 mw during 300- μ sec pulses.

621.385.832.032.2 3660

Space-Charge-Grid High-Transconductance Guns—P. H. Gleichauf. (*Proc. IRE*, vol. 46, p. 1542; August, 1958.) Brief description of the development of a CR tube gun capable of delivering a screen current of 400 μ a at a drive voltage of less than 7 volts.

621.385.832.032.36 3661

The Screen Efficiency of Sealed-Off High-Speed-Oscillograph Cathode-Ray Tubes—R. Feinberg. (*Proc. IEE*, vol. 105, pp. 370-372; July, 1958.) Factors affecting efficiency are summarized. Reduced screen efficiency is due to energy lost by nonradiative dissipation.

MISCELLANEOUS

551.58:621.3.002 3662

A Contribution to the Climatic Classification of Technical Apparatus—H. Burchard and G. Hoffmann. (*Elektrotech. Z., Ed. A*, vol. 79, pp. 315-321; May 1, 1958.) A world map of climatic zones is given which is based on a statistical analysis of maximum and minimum temperatures, and the distribution of population density in these zones is tabulated. A simplified classification of climates is derived so that design and manufacture of equipment can be planned for the widest distribution combined with maximum economy.



Index to

PROCEEDINGS OF THE IRE

Volume 46, 1958

Contents of Issues.....	2
Index to Authors.....	7
Index to Subjects.....	8
Nontechnical Index.....	13
Index to Book Reviews.....	17



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PROCEEDINGS OF THE IRE

CONTENTS OF VOLUME 46-1958

Volume 46, Number 1, January, 1958

Poles and Zeros.....	1
Donald G. Fink, President, 1958.....	2
Introduction to Radio Astronomy, <i>F. T. Haddock</i>	3
The Discovery and Identification by Karl Guthe Jansky of Electromagnetic Radiation of Extraterrestrial Origin in the Radio Spectrum, <i>C. M. Jansky, Jr.</i>	13
Early Radio Astronomy at Wheaton, Illinois, <i>G. Reber</i>	15
The Telescope Program for the National Radio Astronomy Observatory at Green Bank, West Virginia, <i>R. M. Emberson and N. L. Ashton</i>	23
Noise Levels at the National Radio Astronomy Observatory, <i>J. W. Finlay</i>	35
Radio Astronomy at the Meudon Observatory, <i>E. J. Blum, J. F. Denisse, and J. L. Steinberg</i>	39
Considerations in High-Sensitivity Microwave Radiometry, <i>P. D. Strum</i>	43
A Broad-Band Microwave Source Comparison Radiometer for Advanced Research in Radio Astronomy, <i>F. D. Drake and H. I. Thure</i>	53
Present and Future Capabilities of Microwave Crystal Receivers, <i>C. T. McCoy</i>	61
A High Resolution Radio Telescope for Use at 3.5 M, <i>B. Y. Mills, A. G. Little, K. V. Sheridan, and O. B. Slee</i>	67
The Sydney 19.7-MC Radio Telescope, <i>C. A. Shain</i>	85
An Antenna Array for Studies in Meteor and Radio Astronomy at 13 Meters, <i>P. B. Gallagher</i>	89
Radio Telescope Antennas of Large Aperture, <i>J. D. Kraus</i>	92
Radio Interferometry of Discrete Sources, <i>R. N. Bracewell</i>	97
Restoration in the Presence of Errors, <i>R. N. Bracewell</i>	106
Discussion of 10.7-CM Solar Radio Flux Measurements and an Estimation of the Accuracy of Observations, <i>W. J. Medd and A. E. Covington</i>	112
A Method of Calibrating Centimetric Radiometers Using a Standard Noise Source, <i>J. S. Hey and V. A. Hughes</i>	119
Measurements of Solar Radiation and Atmospheric Attenuation at 4.3-Millimeters Wavelength, <i>R. J. Coates</i>	122
Scanning the Sun with a Highly Directional Array, <i>W. N. Christensen and D. S. Mathewson</i>	127
A Dynamic Spectrum Analyzer for Solar Studies, <i>J. Goodman and M. Lehenbaum</i>	132
A Wide-Band Antenna System for Solar Noise Studies, <i>H. Jasik</i>	135
The Radio Spectrum of Solar Activity, <i>A. Maxwell, G. Swarup, and A. R. Thompson</i>	142
Studies at the McMath-Hulbert Observatory of Radio Frequency Radiation at the Time of Solar Flares, <i>H. W. Dodson</i>	149
A Swept-Frequency Interferometer for the Study of High-Intensity Solar Radiation at Meter Wavelengths, <i>J. P. Wild and K. V. Sheridan</i>	160
Radio Astronomy Polarization Measurements, <i>M. H. Cohen</i>	172
The Cornell Radio Polarimeter, <i>M. H. Cohen</i>	183
A Time-Sharing Polarimeter at 200 MC, <i>S. Suzuki and A. Tsuchiya</i>	190
A Polarimeter in the Microwave Region, <i>K. Akabane</i>	194
Critical Frequency, Refractive Index, and Cone of Escape in the Solar Corona, <i>R. N. Bracewell and C. V. Stelford</i>	198
Radio Sources and the Milky Way at 440 MC, <i>N. G. Roman and B. S. Yapple</i>	199
Flux Measurements of Cassiopeia A and Cygnus A between 18.5 MC and 107 MC, <i>H. W. Wells</i>	205
The Distribution of Cosmic Radio Background Radiation, <i>H. C. Ko</i>	208
A Galactic Model for Production of Cosmic Rays and Radio Noise, <i>L. Marshall</i>	215
Absorption Techniques as a Tool for 21-CM Research, <i>A. E. Lilley and E. F. McClain</i>	221
Hydrogen Line Study of Stellar Associations and Clusters, <i>T. K. Menon</i>	230
Extragalactic 21-CM Line Studies, <i>D. S. Heeschen and N. H. Dieter</i>	234
Excitation of the Hydrogen 21-CM Line, <i>G. B. Field</i>	240
Spectral Lines in Radio Astronomy, <i>A. H. Barrett</i>	250
Measurements of Planetary Radiation at Centimeter Wavelengths, <i>C. H. Mayer, T. P. McCullough, and R. M. Sloanaker</i>	260
Planetary and Solar Radio Emission at 11 Meters Wavelength, <i>J. D. Kraus</i>	266
Radio Emission from Comet 1956 h on 600 MC, <i>R. Coutres, J. Huanaeris, and A. Koeckelenbergh</i>	274
Lunar Thermal Radiation at 35 KMC, <i>J. E. Gibson</i>	280
Lunar Radio Echoes, <i>J. H. Trexler</i>	286
Radar Echoes from the Moon at a Wavelength of 10 CM, <i>B. S. Yapple, R. H. Bruton, K. J. Craig, and N. G. Roman</i>	293
The Use of Radio Stars to Study Irregular Refraction of Radio Waves in the Ionosphere, <i>H. G. Booker</i>	298
An Investigation of the Perturbations Imposed Upon Radio Waves Penetrating the Ionosphere, <i>R. S. Lawrence</i>	315
A Phase Tracking Interferometer, <i>H. Penfield</i>	321
Radio Astronomy Measurements at VHF and Microwaves, <i>J. Aarons, W. R. Barron, and J. P. Castelli</i>	325
Some Measurements of High-Latitude Ionospheric Absorption Using Extraterrestrial Radio Waves, <i>C. G. Little and H. Leinbach</i>	334

Cosmical Electrodynamics, <i>J. H. Piddington</i>	349
Correspondence:	
The Effects on Radio Astronomical Observations Due to Longitudinal Propagation in the Presence of Field-Aligned Ionization, <i>S. Rush and L. Colin</i>	356
Launching IGY Satellites, <i>W. H. Finlay</i>	357
Mobile Single-Sideband Equipment, <i>R. E. Morrow</i>	357
Space-Charge Waves Along Magnetically-Focused Electron Beams, <i>W. W. Rigrod and J. Labus</i>	358
A Plea for Maximum Utility in Government Contract Reports Covering Research and Development, <i>E. W. Herold</i>	360
Properties of Ion Filled Waveguides, <i>L. D. Smullin and P. Chorney</i>	360
On the Forward Characteristic of Semiconductor Diodes, <i>H. L. Armstrong</i>	361
Poles and Zeros Squared, <i>A. Papoulis</i>	361
Effect of Correlation on Combiner Diversity, <i>K. S. Packard</i>	362
Contributors.....	364
IRE News and Radio Notes.....	374
Books:	
"Solid State Physics," by A. J. Dekker, <i>Reviewed by F. Herman</i>	379
"The Science of Engineering Materials," ed. by J. E. Goldman, <i>Reviewed by L. T. DeVore</i>	379
"Acoustical Engineering," by H. F. Olson, <i>Reviewed by B. B. Bauer</i>	380
Abstracts of IRE TRANSACTIONS.....	383
Abstracts and References.....	386

Volume 46, Number 1, February, 1958

Scanning the Issue.....	402
Poles and Zeros.....	403
Carl E. Granqvist, Vice-President, 1958.....	404
Microwave Antenna and Waveguide Techniques Before 1900, <i>J. F. Roman</i>	405
Ghost Modes in Imperfect Waveguides, <i>E. T. Jaynes</i>	416
High-Frequency Crystal Filter Design Techniques and Applications, <i>D. I. Kosowsky</i>	419
Experimental 8-MM Klystron Power Amplifiers, <i>T. J. Bridges and H. J. Curnow</i>	430
FM Demodulator Time-Constant Requirements for Interference Rejection, <i>E. J. Baghdady</i>	432
A High-Power Periodically Focused Traveling-Wave Tube, <i>O. T. Purl, J. R. Anderson, and G. R. Brewer</i>	441
Index to IRE Standards on Definitions of Terms, 1942-1957.....	449
Measurement of the Radar Cross Section of a Man, <i>F. V. Schultz, R. C. Burgener, and S. King</i>	476
IRE Standards on Television: Measurement of Luminance Signal Levels, 1958.....	482
Theory of Networks of Linearly Variable Resistances, <i>H. Levenslein</i>	486
Correspondence:	
A Parametric Electron Beam Amplifier, <i>T. J. Bridges</i>	494
On the Earth Geometry—A Theorem, <i>K. Toman</i>	495
Behavior of Noise Figure in Junction Transistors, <i>W. N. Coffey</i>	495
Electrolytic Tank Design of Electron Guns with Curved Electron Trajectories, <i>E. J. Cook</i>	497
Space-Charge-Balanced Hollow Beam with Uniform Charge Distribution, <i>M. Chodorow and C. Süsskind</i>	497
Design of Three-Resonator Dissipative Band-Pass Filters Having Minimum Insertion Loss, <i>M. Dishal, B. Sellers, J. J. Taub, and B. F. Bogner</i>	498
Space-Frequency Equivalence, <i>W. E. Kock and J. L. Stone</i>	499
Thermal Properties of Tungsten vs Copper for Electron Tube Delay Lines, <i>R. A. Paananen</i>	500
Microwave Magnetic Field in Dielectric-Loaded Coaxial Line, <i>B. J. Duncan, L. Swern, and K. Tomiyasu</i>	500
Carrier Mobilities at Low Injection Levels, <i>J. A. Hoerni</i>	502
Hyperbolic Analogs, <i>M. J. Hellstrom</i>	502
Contributors.....	503
IRE News and Radio Notes.....	505
Books:	
"Microwave Measurements," by E. L. Ginzton, <i>Reviewed by A. B. Crawford</i>	508
"Analytical Design of Linear Feedback Controls," by G. C. Newton, Jr., L. A. Gould, and J. F. Kaiser, <i>Reviewed by A. M. Hopkin</i>	508
"Nomograms of Complex Hyperbolic Functions," 2nd ed., by Jorgen Rybner, <i>Reviewed by M. Katzin</i>	509
"Solid State Physics, Vol. IV," ed. by F. Seitz and D. Turnbull, <i>Reviewed by L. T. DeVore</i>	509
Scanning the TRANSACTIONS.....	510
Abstracts of IRE TRANSACTIONS.....	512
Abstracts and References.....	516

Volume 46, Number 3, March, 1958

Scanning the Issue.....	530
Poles and Zeros.....	531
W. R. G. Baker, Winner of the 1958 Founders Award.....	532
Albert W. Hull, Winner of the 1958 Medal of Honor.....	533
Electronics: What's Coming After the Missile Age? <i>W. R. G. Baker</i>	534

Thermoelectric Effects, <i>F. E. Jaumot, Jr.</i>	538	Satellite Doppler Measurements, <i>M. Bernstein, G. H. Gougoulis, O. P. Layden, W. T. Scott, and H. D. Tanzman</i>	782
A Communication Technique for Multipath Channels, <i>R. Price and P. E. Green, Jr.</i>	555	Invention and Insight, <i>R. E. Mueller</i>	783
Low Noise Tunable Preamplifiers for Microwave Receivers, <i>M. R. Currie and D. C. Forster</i>	570	Germanium N-P-I-N Junction Transistor Triodes, <i>D. M. Unger and A. Amalium</i>	783
Atmospheric Noise Interference to Short-Wave Broadcasting, <i>S. V. C. Aiyar</i>	580	High-Frequency Magnetic Permeability Measurements Using Toroidal Coils, <i>R. D. Harrington and R. C. Powell</i>	784
Theory of Junction Diode and Junction Transistor Noise, <i>A. van der Ziel and A. G. T. Becking</i>	589	Passive Repeater Using Double Flat Reflectors, <i>F. Cappuccini and F. Gasparini</i>	784
Ferrite Microwave Detector, <i>D. Jaffe, J. C. Cachetis, and N. Karayianis</i>	594	Observations of Magneto-Ionic Duct Propagation Using Man-Made Signals of Very Low Frequency, <i>R. A. Helliwell and E. Gehrels</i>	785
The Effects of Short Duration Neutron Radiation on Semiconductor Devices, <i>W. V. Behrens and J. M. Shaul</i>	601	Tuning a Probe in a Slotted Line, <i>J. I. Caicoya</i>	787
Optimum Filters with Monotonic Response, <i>A. Papoulis</i>	606	Cutoff Phenomena in Transversely Magnetized Ferrites, <i>R. F. Soohoo</i>	788
Correspondence:		Contributors.....	790
Unusual Propagation at 40 MC from the USSR Satellite, <i>H. W. Wells</i>	610	Scanning the TRANSACTIONS.....	792
A Note on Some Signal Characteristics of Sputnik I, <i>J. D. Kraus and J. S. Athus</i>	610	Books:	
Detection of Sputniks I and II by CW Reflection, <i>J. D. Kraus</i>	611	"Stereophonic Sound," by N. H. Crowhurst, <i>Reviewed by B. B. Bauer</i>	794
The Last Days of Sputnik I, <i>J. D. Kraus</i>	612	"Progress in Semiconductors, Volume Two," ed. by A. F. Gibson, P. Aigrain, and R. E. Burgess, <i>Reviewed by L. T. DeVore</i>	794
Noise Output of Balanced Frequency Discriminator, <i>D. Slepian</i>	614	"The Ionosphere," by Karl Rawer, <i>Reviewed by Wolfgang Pfister</i>	795
An Improved Operational Amplifier, <i>R. Nitzberg</i>	614	"Digital Computer Components and Circuits," by R. K. Richards, <i>Reviewed by W. B. Cagle</i>	796
The Effect of Beam Position on Deflection in Slit Lenses, <i>L. A. Harris</i>	615	"Elektronenröhren," by M. J. O. Strutt, <i>Reviewed by W. H. von Aulock</i>	796
An Extended General Network Theorem on Rectification, <i>H. Stockman</i>	615	"Notes on Analog-Digital Conversion Techniques," ed. by A. K. Süsskind, <i>Reviewed by C. T. Leondes</i>	796
Variation of Junction Transistor Current Amplification Factor with Emitter Current, <i>A. W. Matz</i>	616	"Scientific and Technical Translating and Other Aspects of the Language Problem," by UNESCO, <i>Reviewed by W. N. Locke</i>	797
Efficiency of Large Antennas in O/H Links, <i>G. De Vito</i>	617	Recent Books.....	797
High-Frequency Quartz Filter Crystals, <i>R. Bechmann</i>	617	Abstracts of IRE TRANSACTIONS.....	798
Design of a Conical Taper in Circular Waveguide System Supporting H ₁₁ Mode, <i>L. Solymar</i>	618	Abstracts and References.....	806
Measuring Noise Figures of Transistor Amplifiers, <i>A. Y. Anouchi</i>	619	1957 IRE TRANSACTIONS INDEX.....	818
Contributors.....	619	IRE News and Radio Notes.....	14A
1958 IRE National Convention Program.....	622		
IRE News and Radio Notes.....	658		
Books:			
"Transistor Circuits and Applications," by J. M. Carroll, <i>Reviewed by R. P. Burr</i>	662	Poles and Zeros.....	819
"Introduction to Transistor Circuits," by E. H. Cooke-Yarborough, <i>Reviewed by H. E. Tompkins</i>	662	Kenneth V. Newton, Director, 1957-1958.....	820
"Receiving Aerial Systems," by I. A. Davidson, <i>Reviewed by C. E. Smilli</i>	662	Scanning the Issue.....	821
"An Introduction to Probability Theory and Its Applications," vol. I, 2nd ed., by William Feller, <i>Reviewed by R. M. Fano</i>	662	Section Survey of IRE Editorial Policies.....	822
"Electronic Components Handbook," ed. by Keith Henney and Craig Walsh, <i>Reviewed by R. R. Batcher</i>	662	JTAC—Ten Years of Service, <i>D. G. Fink</i>	823
"Selection and Application of Metallic Rectifiers," by S. P. Jackson, <i>Reviewed by J. T. Cataldo</i>	663	A Statistical Description of Coincidences Among Random Pulse Trains, <i>S. Stein and D. Johansen</i>	827
"Impulse und Schaltvorgänge in der Nachrichtentechnik," by Heinrich Kaden, <i>Reviewed by G. C. Sziklas</i>	663	Transient Response of Drift Transistors, <i>R. C. Johnston</i>	830
"Engineering Electronics," by J. D. Ryder, <i>Reviewed by J. J. Gershon</i>	663	Terminal Properties of Magnetic Cores, <i>T. C. Chen and A. Papoulis</i>	839
"Fundamentals of Electron Devices," by K. R. Spangenberg, <i>Reviewed by L. J. Giacoletto</i>	664	Some General Properties of Nonlinear Elements. II. Small Signal Theory, <i>H. E. Rowe</i>	850
"Mathematics and Computers," by G. R. Stibitz and J. A. Larrivee, <i>Reviewed by J. R. Weiner</i>	664	Very Low-Noise Traveling-Wave Amplifier, <i>E. W. Kinaman and M. Magid</i>	861
Recent Books.....	664	New Applications of Impedance Networks as Analog Computers for Electronic Space Charge and for Semiconductor Diffusion Problems, <i>G. Cremosnik, A. Frei, and M. J. O. Strutt</i>	868
Scanning the TRANSACTIONS.....	665	IRE Standards on Solid-State Devices: Methods of Testing Point-Contact Transistors for Large-Signal Applications, 1958.....	878
Abstracts of IRE TRANSACTIONS.....	669	Carrier-to-Noise Statistics for Various Carrier and Interference Characteristics, <i>K. K. Clarke and J. Cohn</i>	889
Abstracts and References.....	671	Simultaneous Asynchronous Oscillations in Class-C Oscillators, <i>M. I. Disman and W. A. Edson</i>	895
	676	Theoretical Diversity Improvement in Frequency-Shift Keying, <i>J. N. Pierce</i>	903
		Correspondence:	
		The President Smiles, <i>W. Eckles</i>	910
		WWV Standard Frequency Transmissions, <i>W. D. George</i>	910
		A New Type of Low-Noise Electron Gun for Microwave Tubes, <i>M. R. Currie</i>	911
		S-Band Traveling-Wave Tube with Noise Figure Below 4 DB, <i>M. Caullon and G. E. St. John</i>	911
		Design Considerations for Circular Maser Systems, <i>F. R. Arams and G. Krayner</i>	912
		System-Noise Measurement of a Solid-State Maser, <i>A. L. McWhorter and F. R. Arams</i>	913
		Re-Invention by Young Engineers, <i>E. W. Herold</i>	914
		Leakage in Foil Solenoids, <i>G. M. Clarke and G. B. Lees</i>	914
		Lightning Enhancement of a VHF Tropospheric Scatter Signal, <i>C. R. Graf</i>	915
		Analysis of Sampled-Data Systems Containing Nonlinear Element, <i>J. Tou</i>	915
		Doppler Equation for Earth Satellite Measurements, <i>A. Schwartzman and P. D. Stahl</i>	915
		A UHF Solid-State Maser, <i>R. H. Kingston</i>	916
		A Property of Ladder Networks, <i>A. H. Zemanian</i>	916
		Translation of Foreign Articles, <i>E. L. Soohoo and T. O. Jones</i>	917
		Mixer Crystal Noise, <i>N. Houliou</i>	917
		Diode Space and Space Charge, <i>P. A. Clavier</i>	918
		Error Rates in Data Transmission, <i>S. Reiger</i>	919
		Common Emitter Transistor Amplifiers, <i>D. F. Dion</i>	920
		Electromagnetic Analogs for the Gravitational Fields in the Vicinity of a Satellite, <i>W. D. White</i>	920
		Off-Path Propagation at VHF, <i>V. C. Pineo</i>	922
		Experimental Check of Formulas for Capacitance of Shielded Balanced-Pair Transmission Line, <i>B. G. King, J. McKenna, and G. Raisbeck</i>	922
		Contributors.....	923
		Scanning the TRANSACTIONS.....	926
		Books:	
		"An Introduction to Semiconductors," by W. C. Dunlap, Jr., <i>Reviewed by S. N. Van Voorhis</i>	927

Volume 46, Number 4, April, 1958

Poles and Zeros.....	689		
John D. Ryder, Editor, 1958.....	690		
Scanning the Issue.....	691		
A Short Survey of Radio and Electronics in Colombia, <i>T. J. Meek</i>	692		
A Transistorized 150-MC FM Receiver, <i>W. J. Giguere</i>	693		
A Traveling-Wave Ferromagnetic Amplifier, <i>P. K. Tien and H. Suhl</i>	700		
Parametric Amplification of Space Charge Waves, <i>W. H. Louisell and C. F. Quate</i>	707		
A Gallium Arsenide Microwave Diode, <i>D. A. Jenny</i>	717		
Some Applications of Ferrites to Microwave Switches, Phasers, and Isolators, <i>A. C. Brown, R. S. Cole, and W. N. Honeyman</i>	722		
Theory of Stronger-Signal Capture in FM Reception, <i>E. J. Baghdady</i>	728		
Exact Ladder Network Design Using Low-Q Coils, <i>L. Weinberg</i>	739		
Minimum Energy Triggering Signals, <i>L. A. Beattie</i>	751		
Some Studies on Delayed Feedback Circuits, <i>H. Seki</i>	758		
IRE Standards on Piezoelectric Crystals: Determination of the Elastic, Piezoelectric, and Dielectric Constants—The Electro-mechanical Coupling Factor, 1958.....	764		
Correction to "Radio Interferometry of Discrete Sources" and "Restoration in the Presence of Errors," <i>R. N. Bracewell</i>	778		
Correspondence:			
Bridge Method of Measuring Noise in Low-Noise Devices at Radio Frequencies, <i>K. S. Champlin</i>	779		
A Reactance Theorem for Antennas, <i>L. Solymar</i>	779		
Extension of Boolean Algebra for Analysis of Mixed-Switch Diode Circuits, <i>B. Beizer</i>	779		
The Switching Time of the Cryotron, <i>A. Aharoni, E. H. Frei, and S. Shrikman</i>	780		
A History of Some Foundations of Modern Radio-Electronic Technology, <i>S. M. Aisenstein</i>	780		
Aperture Correction for Instrumentation Systems, <i>J. Ollerman</i>	781		
Transistor Cutoff Frequency Measurement, <i>L. G. Cripps</i>	781		
Spectral Analysis, <i>R. C. Moody</i>	782		

"Handbook of Noise Control," ed. by C. M. Harris, <i>Reviewed by V. Work</i>	927
"Industrial Electronics Handbook," 2nd ed., and "Industrial Electronics Circuits," by R. Kretzmann, <i>Reviewed by W. L. Atwood</i>	927
"Basic Electric Circuit Theory," by W. W. Lewis with the assistance of C. F. Goodheart, <i>Reviewed by A. B. Giordano</i>	928
"Closed Circuit TV System Planning," by M. A. Mayers and R. D. Chipp, <i>Reviewed by F. J. Bingley</i>	928
"Electrical Discharges in Gases," by F. M. Penning, <i>Reviewed by J. D. Cobine</i>	929
"Passive Network Synthesis," by J. E. Storer, <i>Reviewed by P. F. Ording</i>	929
"Solid State Physical Electronics," by Aldert van der Ziel, <i>Reviewed by A. R. Moore</i>	929
Recent Books	929
Abstracts of IRE TRANSACTIONS.....	930
Abstracts and References.....	933
IRE News and Radio Notes.....	14A

Volume 46, Number 6, June, 1958

Poles and Zeros.....	947
William H. Doherty, Director, 1958-1960.....	948
Scanning the Transistor Issue, S. J. Angello.....	949
Comments on Implications of Transistor Research, J. Bardeen.....	952
Essay on the Tenth Anniversary of the Transistor, W. H. Brattain.....	953
An Invited Essay on Transistor Business, W. Shockley.....	954
The Technological Impact of Transistors, J. A. Morton and W. J. Pielenpol.....	955
The Status of Transistor Research in Compound Semiconductors, D. A. Jenny.....	959
Review of Other Semiconductor Devices, S. J. Angello.....	968
Electrons, Holes, and Traps, W. Shockley.....	973
Recombination in Semiconductors, G. Bemski.....	990
Noise in Semiconductors and Photoconductors, K. M. van Vliet.....	1004
Noise in Junction Transistors, A. van der Ziel.....	1019
The Effects of Neutron Irradiation on Germanium and Silicon, G. C. Messenger and J. P. Spratt.....	1038
Irradiation of P-N Junctions with Gamma Rays: A Method for Measuring Diffusion Lengths, R. Grennemaier.....	1045
Formation of Junction Structures by Solid-State Diffusion, F. M. Smits.....	1049
The Preparation of Semiconductor Devices by Lapping and Diffusion Techniques, H. Nelson.....	1062
Outdiffusion as a Technique for the Production of Diodes and Transistors, J. Halpern and R. H. Rediker.....	1068
The Evolution of the Theory for the Voltage-Current Characteristic of P-N Junctions, J. L. Moll.....	1076
Analog Solution of Space-Charge Regions in Semiconductors, L. J. Giacomello.....	1083
Correction to "The Use of Radio Stars to Study Irregular Refraction of Radio Waves in the Ionosphere," H. G. Booker.....	1085
Germanium and Silicon Rectifiers, H. W. Henkels.....	1086
The Potential of Semiconductor Diodes in High-Frequency Communications, A. Uhlir, Jr.....	1099
New Concepts in Microwave Mixer Diodes, G. C. Messenger.....	1116
Narrow Base Germanium Photodiodes, D. E. Sawyer and R. H. Rediker.....	1122
Advances in the Understanding of the P-N Junction Triode, R. L. Prichard.....	1130
Lumped Models of Transistors and Diodes, J. G. Linvill.....	1141
Two-Dimensional Current Flow in Junction Transistors at High Frequencies, R. L. Prichard.....	1152
Construction and Electrical Properties of a Germanium Alloy-Diffused Transistor, P. J. W. Jochems, O. W. Memelink, and L. J. Tummers.....	1161
Technology of Micro-Alloy Diffused Transistors, C. G. Thornton and J. B. Angell.....	1166
Junction Transistor Short Circuit Current Gain and Phase Determination, D. E. Thomas and J. L. Moll.....	1177
Correction to "Exact Ladder Network Design Using Low-Q Coils," L. Weinberg.....	1184
Power Transistors, M. A. Clark.....	1185
Measurement of Transistor Thermal Resistance, B. Reich.....	1204
Measurement of Internal Temperature Rise of Transistors, J. T. Nelson and J. E. Iuversen.....	1207
A Five-Watt Ten-Megacycle Transistor, J. T. Nelson, J. E. Iuversen, and F. Keywell.....	1209
The Blocking Capability of Alloyed Silicon Power Transistors, R. Emeis and A. Herlet.....	1216
The Effective Emitter Area of Power Transistors, R. Emeis, A. Herlet, and F. Spenke.....	1220
The Electrical Characteristics of Silicon P-N-P-N Triodes, I. M. Mackintosh.....	1229
Multiterminal P-N-P-N Switches, R. W. Aldrich and N. Holonyak.....	1236
The Application of Transistors to Computers, R. A. Henle and J. L. Walsh.....	1240
Application of Transistors in Communications Equipment, D. D. Holmes.....	1255
Transistor Monostable Multivibrators for Pulse Generation, J. J. Simon.....	1260
A Design Basis for Junction Transistor Oscillator Circuits, D. F. Page.....	1271
Properties of Silicon and Germanium: II, E. M. Corwell.....	1281
Correspondence:	
Parametric Amplification of the Fast Electron Wave, R. Adler.....	1300
Experimental Characteristics of a Microwave Parametric Amplifier Using a Semiconductor Diode, H. Heffner and K. Koizabue.....	1301

Noise Figure Measurements on Two Types of Variable Reactance Amplifiers Using Semiconductor Diodes, G. F. Herrmann, M. Uenohara, and A. Uhlir, Jr.....	1301
A Low-Noise Wide-Band Reactance Amplifier, B. Salzberg and E. W. Sard.....	1303
Measurement of the Correlation Between Flicker Noise Sources in Transistors, E. R. Chenette.....	1304
On the Effect of Base Resistance and Collector-to-Base Overlap on the Saturation Voltages of Power Transistors, H. G. Rudenberg.....	1304
Voltage Feedback and Thermal Resistance in Junction Transistors, J. J. Sparkes.....	1305
Microwave Transients from Avalanche Silicon Diodes, J. L. Moll, A. Uhlir, Jr., and B. Senitzky.....	1306
A Harmonic Generator by Use of the Nonlinear Capacitance of Germanium Diode, S. Kita.....	1307
On Junctions Between Semiconductors Having Different Energy Gaps, H. L. Armstrong.....	1307
Arc Prevention Using P-N Junction Reverse Transient, B. Zarwyn.....	1308
Improved Keep-Alive Design for TR Tubes, D. Walsh.....	1309
WWV Standard Frequency Transmissions, W. D. George.....	1309
Contributors.....	1310
Scanning the TRANSACTIONS.....	1317
Report of the Secretary—1957.....	1318
Books:	
"Engineering College Research Review—1957," ed. by Renato Contini, <i>Reviewed by H. H. Goode</i>	1322
"Transistor Electronics," by David DeWitt and A. L. Rossoff, <i>Reviewed by A. P. Stern</i>	1322
"Radio Aids to Air Navigation," by J. H. H. Grover, <i>Reviewed by H. Busignies</i>	1323
"Elements of Magnetic Tape Recording," by N. M. Haynes, <i>Reviewed by F. A. Comer</i>	1323
"Logical Design of Digital Computers," by Montgomery Phister, Jr., <i>Reviewed by R. A. Tracy</i>	1323
"L'Automatique des Informations," by F. H. Raymond, <i>Reviewed by J. P. Jeanneney</i>	1324
"The Management Approach to Electronic Digital Computers," by J. S. Smith and "Automation and Management," by J. R. Bright, <i>Reviewed by J. J. Lamb</i>	1324
"The Measurement of Colour," by W. D. Wright, <i>Reviewed by W. T. Wintringham</i>	1325
Abstracts of IRE TRANSACTIONS.....	1325
Abstracts and References.....	1332
IRE News and Radio Notes.....	14A

Volume 46, Number 7, July, 1958

Poles and Zeros.....	1347
Gordon S. Brown, Director, 1958-1960.....	1348
Scanning the Issue.....	1349
Twelfth General Assembly of International Scientific Radio Union, F. H. Dickson.....	1350
What Is URSI? H. W. Wells.....	1351
Address of Welcome, D. W. Bronk.....	1352
Report on URSI Commission I—Radio Measurement Methods and Standards, E. Weber.....	1354
Report on URSI Commission II—Tropospheric Radio Propagation, J. B. Smyth.....	1358
Report on URSI Commission III—Ionospheric Radio Propagation, L. A. Manning.....	1362
Report on URSI Commission IV—Radio Noise of Terrestrial Origin, H. E. Dinger.....	1366
Report on URSI Commission V—Radio Astronomy, F. T. Had-dock.....	1373
Report on URSI Commission VI—Radio Waves and Circuits, E. C. Jordan.....	1376
Report on URSI Commission VII—Radio Electronics, W. G. Shepherd.....	1381
A Parametric Amplifier Using Lower-Frequency Pumping, K. K. N. Chang and S. Bloom.....	1383
A Ferromagnetic Resonance Frequency Converter, K. M. Poole and P. K. Tien.....	1387
A Mathematical Analysis of the Kahn Compatible Single-Side-band System, J. P. Costas.....	1396
Investigation of Long-Distance Overwater Tropospheric Propagation at 400 MC, H. E. Dinger, W. E. Garner, D. H. Hamilton, Jr., and A. E. Teachman.....	1401
The Hall Effect and Its Application to Microwave Power Measurement, H. M. Barlow.....	1411
Surface Waves, H. M. Barlow.....	1413
Correction to "IRE Standards on Television: Measurement of Luminance Signal Levels, 1958".....	1417
Supplement to "IRE Standards on Receivers: Methods of Measurement of Interference Output of Television Receivers in the Range of 300 to 10,000 KC, 1954 (Standard 54 IRE 17.51)".....	1418
Correspondence:	
WWV Standard Frequency Transmissions, W. D. George.....	1420
Pumping to Extend Traveling-Wave-Tube Frequency Range, L. D. Buchmiller and G. Wade.....	1420
Mixed Garnets for Nonreciprocal Devices at Low Microwave Frequencies, B. Ancker-Johnson and J. J. Rowley.....	1421
Design Theory for Depletion Layer Transistors, J. E. Rosenthal and W. W. Gärtner.....	1422
On the Transmission Error Function for Meteor-Burst Communication, G. F. Montgomery.....	1423
Harmonic Generation at Microwave Frequencies Using Field-Emission Cathodes, J. R. Fontana and H. J. Shaw.....	1424

First Meeting on Radio Climatology, <i>B. R. Bean</i>	1425
A Possible Simplification of Stereophonic Audio Systems, <i>A. Sobel</i>	1426
Noise in Mixer Tubes, <i>A. van der Ziel and R. L. Walters</i>	1426
The Forward Switching Transient in Semiconductor Diodes at Large Currents, <i>F. S. Barnes</i>	1427
On the Codification of Lagrangian Formulation, <i>H. E. Koenig and W. A. Blackwell</i>	1428
Comment on "A Mathematical Analysis of the Kahn Compatible Single-Sideband System," <i>L. R. Kahn</i>	1429
On the Mass Education of Scientists, <i>B. F. Miessner</i>	1430
Contributors.....	1431
Scanning the TRANSACTIONS.....	1434
Books:	
"Propagation Troposphérique," by Georges Boudouris, <i>Reviewed by G. Deschamps</i>	1435
"Fundamental Principles of Transistors," by J. Evans, <i>Reviewed by F. H. Blecher</i>	1435
"Synthesis of Passive Networks," by E. A. Guillemin, <i>Reviewed by S. Darlington</i>	1436
"The Ultra High Frequency Performance of Receiving Tubes," by W. E. Benham and I. A. Harris, <i>Reviewed by R. D. Wilson</i>	1436
"Analysis and Control of Nonlinear Systems," by Y. A. Ku, <i>Reviewed by T. M. Stout</i>	1436
"Basic Electrical Engineering," by R. H. Nau, <i>Reviewed by A. V. Eastman</i>	1437
"Transistor Physics and Circuits," by R. L. Riddle and M. P. Ristenbatt, <i>Reviewed by A. Warnick</i>	1437
"The Theory of Networks in Electrical Communication and Other Fields," by F. E. Rogers, <i>Reviewed by E. A. Guillemin</i>	1437
"Technical Report Writing," by J. W. Souther, <i>Reviewed by J. D. Chapline</i>	1438
"The Encyclopedia of Radio and Television," <i>Reviewed by P. Mertz</i>	1438
Abstracts of IRE TRANSACTIONS.....	1438
Abstracts and References.....	1444
IRE News and Radio Notes.....	14A

Volume 46, Number 8, August, 1958

Poles and Zeros.....	1459
Glenn A. Fowler, Director, 1958-1959.....	1460
Scanning the Issue.....	1461
Batteries, <i>C. K. Morehouse, R. Glicksman, and G. S. Lozier</i>	1462
The Resatron as a 200-MC Power Amplifier, <i>E. B. Tucker, H. J. Schulte, E. A. Day, and E. E. Lampi</i>	1483
Atmospheric Effects on VHF and UHF Propagation, <i>G. H. Millman</i>	1492
Atmospheric Noise Interference to Medium Wave Broadcasting, <i>S. V. Aiyar</i>	1502
Suppression of Undesired Radiation of Directional HF Antennas and Associated Feed Lines, <i>H. Brueckmann</i>	1510
Optimum Noise Performance of Linear Amplifiers, <i>H. A. Haus and R. B. Adler</i>	1517
Correction to "Recombination in Semiconductors," <i>G. Bemski</i>	1533
Correspondence:	
Observations of the U. S. Satellites Explorers I and III by CW Reflection, <i>J. D. Kraus, R. C. Higgy, and J. S. Albus</i>	1534
WWV Standard Frequency Transmissions, <i>W. D. George</i>	1534
Continuous Phase Difference Measurements of Earth Satellites, <i>J. W. Herbstreit and M. C. Thompson, Jr.</i>	1535
Semiconductor P-N Junction Radiation Counter, <i>B. Salasberg and K. Siegel</i>	1536
Observed Bunched Electron Current in a Velocity-Modulated Beam, <i>H. Maeda</i>	1536
Design of Transistor Regulated Power Supplies, <i>T. F. Kopaczek</i>	1537
Use of Microwave Ferrite Toroids to Eliminate External Magnets and Reduce Switching Power, <i>M. A. Treuhart and L. M. Silber</i>	1538
A Theorem for Dissipationless Networks, <i>G. Szentirmai</i>	1538
Cutoff Voltage Characteristics of TV Picture Tubes, <i>W. F. Niklas</i>	1539
A Study of Earth Currents Near a VLF Monopole Antenna with a Radial Wire Ground System, <i>J. R. Wail</i>	1539
Design of Video Amplifiers with Stringent Electrical and Mechanical Requirements, <i>J. A. Develet, Jr.</i>	1541
Networks of Fixed and Variable Resistors, <i>H. L. Armstrong</i>	1541
Space-Charge Grid High-Transconductance Guns, <i>P. H. Gleichauf</i>	1542
Contributors.....	1543
Scanning the TRANSACTIONS.....	1545
Books:	
"Physique Electronique des Gaz et des Solides," by Michel Bayet, <i>Reviewed by J. I. Pankove</i>	1546
"The Exploration of Space by Radio," by R. H. Brown and A. C. B. Lovell, <i>Reviewed by F. T. Haddock</i>	1546
"Principles of Electrical Measurements," by H. Buckingham and E. M. Price, <i>Reviewed by G. B. Hoadley</i>	1547
"An Introduction to the Theory of Random Signals and Noise," by W. B. Davenport, Jr., and W. L. Root, <i>Reviewed by W. M. Siebert</i>	1547
"Atmospheric Explorations," ed. by H. G. Houghton, <i>Reviewed by A. W. Straton</i>	1547
"Soviet Education for Science and Technology," by A. G. Korol, <i>Reviewed by E. Weber</i>	1548
"An Introduction to Digital Computers," by R. K. Livesley, <i>Reviewed by W. B. Cagle</i>	1548
"Principles of Electronic Instruments," by G. R. Partridge, <i>Reviewed by W. Richter</i>	1549
"Zone Melting," by W. G. Pfann, <i>Reviewed by D. A. Jenny</i>	1549
"Feedback Control Systems," by O. J. M. Smith, <i>Reviewed by G. S. Axelby</i>	1549

"Electronic Semiconductors," by Eberhard Spence, translated by D. Jenny, H. Kroemer, E. G. Ramberg, and A. H. Sommer, <i>Reviewed by G. C. Dacey</i>	1550
"Photosensors," by W. Summer, <i>Reviewed by F. Koury</i>	1550
"Control Engineer's Handbook," ed. by J. G. Truxal, <i>Reviewed by J. M. Salzer</i>	1551
"Van Nostrand's Scientific Encyclopedia," 3rd ed., <i>Reviewed by G. Shapiro</i>	1551
Recent Books.....	1552
Abstracts of IRE TRANSACTIONS.....	1552
Abstracts and References.....	1556
IRE News and Radio Notes.....	14A

Volume 46, Number 9, September, 1958

Poles and Zeros.....	1571
Donald B. Sinclair, Director, 1958.....	1572
Scanning the Issue.....	1573
Analysis and Experimental Results of a Diode Configuration of a Novel Thermoelectron Engine, <i>G. N. Hatsopoulos and J. Kaye</i>	1574
Sputnik I's Last Days in Orbit, <i>J. D. Kraus and E. E. Dreese</i>	1580
Correction to "Thermoelectric Effects," <i>F. E. Jaumot</i>	1587
Noise in Maser Amplifiers—Theory and Experiment, <i>J. P. Gordon and L. D. White</i>	1588
The Spherical Coil as an Inductor, Shield, or Antenna, <i>H. A. Wheeler</i>	1595
Error Probabilities for Binary Symmetric Ideal Reception through Nonselective Slow Fading and Noise, <i>G. L. Turin</i>	1603
Diffraction by Smooth Cylindrical Mountains, <i>H. E. J. Neugebauer and M. P. Bachynski</i>	1619
Refraction Anomalies in Airborne Propagation, <i>M. S. Wong</i>	1628
A Cathode Test Utilizing Noise Measurements, <i>W. Dahlke and F. Dlouhy</i>	1639
Correction to "IRE Standards on Radio Aids to Navigation: Definition of Terms, 1954".....	1645
IRE Standards on Information Theory: Definitions of Terms, 1958.....	1646
Correspondence:	
Optimum Finite Code Groups, <i>J. E. Storer and R. Turyn</i>	1649
WWV Standard Frequency Transmissions, <i>W. D. George</i>	1649
Storage Capacity in Meteor-Burst Communication Systems, <i>W. A. Helbig</i>	1649
Radio Engineering Use of the Cayley-Klein Model of Three-Dimensional Hyperbolic Space, <i>E. F. Bolinder</i>	1650
Properties of Root Loci, <i>C. S. Lorens</i>	1651
A Proposed Technique for the Improvement of Range Determination with Noise Radar, <i>H. Hochstadt</i>	1652
Estimates of Entropy of a Message Source, <i>C. N. Campopiano</i>	1652
Minimum Weight Solenoid Systems, <i>G. M. Clarke</i>	1652
Various Definitions of the Delta Entities, <i>O. Pankraz</i>	1653
Some Comments on Minimum Triggering Signals, <i>J. L. Dautremont, Jr.</i>	1654
A Low-Noise Nonlinear Reactance Traveling-Wave Amplifier, <i>R. S. Engelbrecht</i>	1655
The Electron Optical Action of an Annular Aperture Lens, <i>L. A. Harris</i>	1655
Pulse Modulation Transmitted through a Linearly Modulated Transit-Time Device, <i>V. Met</i>	1656
Phase Dependence of a Ferromagnetic Microwave Amplifier, <i>W. L. Wherry and F. B. Wang</i>	1657
Analysis of Traveling-Wave Tubes with Tapered Velocity Parameter, <i>D. V. Geppert</i>	1658
Contributors.....	1659
Scanning the TRANSACTIONS.....	1661
Books:	
"Mass Spectroscopy," by H. E. Duckworth, <i>Reviewed by H. C. Matraw</i>	1662
"Introduction to Electromagnetic Engineering," by R. F. Harrington, <i>Reviewed by L. A. Manning</i>	1662
"Transients in Electrical Circuits," by G. V. Lago and D. L. Waidlich, <i>Reviewed by G. B. Herzog</i>	1663
"Modern Computing Methods," <i>Reviewed by L. N. Ridemour</i>	1663
"Einführung in die Mikrowellen-Elektronik Teil II: Lauffeldröhren," by Werner Kleen and Klaus Pöschl, <i>Reviewed by W. J. Albersheim</i>	1663
"Principles of Electricity," (3rd ed.) by Leigh Page and N. I. Adams, Jr., <i>Reviewed by E. T. Jaynes</i>	1664
Abstracts of IRE TRANSACTIONS.....	1665
Abstracts and References.....	1668
IRE News and Radio Notes.....	14A

Volume 46, Number 10, October, 1958

Poles and Zeros.....	1683
Allan B. Oxley, Director, 1957-1958.....	1684
Scanning the Issue.....	1685
The Westrex StereoDisk System, <i>C. C. Davis and J. G. Frayne</i>	1686
ELF—A New Electroluminescent Display, <i>E. A. Sack</i>	1694
The Helitron Oscillator, <i>D. A. Watkins and G. Wada</i>	1700
Guided Wave Propagation in Submillimetric Region, <i>A. E. Karbowiak</i>	1706
Solar Cycle Influence on the Lower Ionosphere and on VHF Forward Scatter, <i>C. Ellyett and H. Leighton</i>	1711
On the Determination of the Electrodes Required to Produce a Given Electric Field Distribution Along a Prescribed Curve, <i>P. T. Kirstein</i>	1716
A Voltage-Sensitive Switch, <i>K. O. Olley, R. F. Shoemaker, and P. J. Franklin</i>	1723
Methods of Measurement of the Parameters of Piezoelectric	

Vibrators, E. A. Gerber and L. F. Koerner.....	1731
Harmonic Generation with Ideal Rectifiers, C. H. Page.....	1738
An Error-Correcting Encoder and Decoder of High Efficiency, J. H. Green, Jr., and R. L. San Soucie.....	1741
A Computer Oriented Toward Spatial Problems, S. H. Unger.....	1744
Distribution of Leakage Flux Around a TWT-Focusing Magnet—A Graphic Analysis, M. S. Glass.....	1751
Correspondence:	
A Low-Noise Electron-Beam Parametric Amplifier, R. Adler, G. Hrbek, and G. Wade.....	1756
A Proposed Technique for the Improvement of Range Determination with Noise Radar, G. L. Turin.....	1757
WWV Standard Frequency Transmissions, W. D. George.....	1758
A Further Note on Differentiability of Autocorrelation Functions, D. G. Brennan, F. J. Beutler, and N. Wiener.....	1758
Some Properties of Lightning Impulses Which Produce Whistlers, R. A. Helliwell, A. G. Jean, and W. L. Taylor.....	1760
Hyperbolic Analogs Using Varistors, G. W. Holbrook.....	1762
Radio Reflections from Satellite-Produced Ion Columns, C. D. Hendricks, Jr., G. W. Swenson, Jr., and R. A. Schorn.....	1763
Estimation of Dissipative Effects in Tchebycheff Symmetrical Filters, D. C. Pawsey.....	1763
Contributors.....	1765
Scanning the TRANSACTIONS.....	1768
Books:	
"The Solid State for Engineers," by Maurice J. Sinnott, Reviewed by J. S. Saby.....	1769
"Circuit Analysis of Transmission Lines," by J. L. Stewart, Reviewed by H. A. Wheeler.....	1769
"Piezoelectricity," by the General Post Office Research Station, Reviewed by H. Jaffe.....	1770
"Nonlinear Control Systems," by R. L. Cosgriff, Reviewed by T. M. Stout.....	1770
"Television in Science and Industry," by V. K. Zworykin, E. G. Ramberg, and L. E. Flory, Reviewed by R. D. Chipp.....	1770
"Principles of Noise," by J. J. Freeman, Reviewed by W. D. White.....	1771
"Introduction to Electromagnetic Fields," by Samuel Seely, Reviewed by A. B. Haines.....	1771
"Le Calcul Analogique par Courants Continus," by Danloux Dumesnils, Reviewed by B. Lippel.....	1771
Recent Books.....	1772
Abstracts of IRE TRANSACTIONS.....	1772
Abstracts and References.....	1780
IRE News and Radio Notes.....	14A

Volume 46, Number 11, November, 1958

Poles and Zeros.....	1795
Ralph I. Cole, Director, 1958-1959.....	1796
Scanning the Issue.....	1797
Electronic Composites in Modern Television, R. C. Kennedy and F. J. Gaskins.....	1798
Transfluxor Controlled Electroluminescent Display Panels, J. A. Rajchman, G. R. Briggs, and A. W. Lo.....	1808
Incoherent Scattering of Radio Waves by Free Electrons with Applications to Space Exploration by Radar, W. E. Gordon.....	1824
Analysis of Millimicrosecond RF Pulse Transmission, M. P. Forrer.....	1830
A Quartz Servo Oscillator, N. Lea.....	1835
Some Generalized Scattering Relationships in Transhorizon Propagation, A. T. Waterman, Jr.....	1842
A Very-Wide-Band Balun Transformer for VHF and UHF, T. R. O'Meara and R. L. Sydnor.....	1848
Nomographs for Designing Elliptic-Function Filters, K. W. Henderson.....	1860
The Annular Geometry Electron Gun, J. W. Schwartz.....	1864
Correspondence:	
Undersea and Underground "Atmospherics," T. Powell.....	1870
On the Choice of Frequencies for Meteor-Burst Communication, M. L. Meeks and J. C. James.....	1871
The Superconductive-Transition Radio-Frequency Mixer and the Problem of Cryotron Switching Time, J. B. Woodford, Jr., and D. Feucht.....	1871
Amplitude Scintillation of Extraterrestrial Radio Waves at Ultra-High Frequency, H. C. Ko.....	1872
Statistical Design and Analysis of Closed-Loop Control Systems with Error Sampling, R. M. Stewart.....	1873
On the Statistics of Filled Vessels, J. L. Stewart.....	1873
Electron-Density Profiles in the Ionosphere During the IGY, R. L. Smith-Rose.....	1874
The Current Amplification of a Junction Transistor as a Function of Emitter Current and Junction Temperature, W. W. Gärtner, R. Hanel, R. Stampfl, and F. Caruso.....	1875
Alternative Detection of Co-Channel FM Signals, H. W. Farris A Series Expansion Method for Finding Approximate Laplace Transforms, W. H. Lucke.....	1876
Effective Collector Capacitance in Transistors, R. Zuleeg.....	1877
Maximum Utility in Government Contract Reports, F. H. Warren and E. W. Herold.....	1878
Proposal for a Maser-Amplifier System Without Nonreciprocal Elements, S. H. Aulter.....	1879
WWV Standard Frequency Transmissions, D. M. Kerns.....	1880
A Communication Technique for Multipath Channels, G. D. Hulst.....	1881
Magnetron Tuning Using a Ferrite Reciprocal Phase Shifter, D. Bush.....	1882
Contributors.....	1882
Scanning the TRANSACTIONS.....	1883
	1885

Books:	
"Faisceaux Hertiens et Systèmes de Modulation," by L. J. Libois, Reviewed by J. B. Lair.....	1886
"Programming for an Automatic Digital Calculator," by K. H. V. Booth, Reviewed by D. Combelic.....	1886
"Switching Circuits and Logical Design," by S. H. Caldwell, Reviewed by R. W. Stuart.....	1887
"Missile Engineering Handbook," by C. W. Besserer, Reviewed by C. H. Hoeppner.....	1887
Abstracts of IRE TRANSACTIONS.....	1888
Abstracts and References.....	1892
IRE News and Radio Notes.....	14A

Volume 46, Number 12, December, 1958

Poles and Zeros.....	1907
E. H. Schulz, Director, 1958-1959.....	1908
Scanning the Issue.....	1909
General Power Relationships for Positive and Negative Nonlinear Resistive Elements, R. H. Pantell.....	1910
Performance of Some Radio Systems in the Presence of Thermal and Atmospheric Noise, A. D. Watt, R. M. Coon, E. L. Maxwell, and R. W. Plush.....	1914
Structure-Determined Gain Band Product of Junction Triode Transistors, J. M. Early.....	1924
IRE Standards on Audio Techniques: Definitions of Terms, 1958.....	1928
Frequency Variations in Short-Wave Propagation, T. Ogawa.....	1934
IRE Standards on Recording and Reproducing: Methods of Calibration of Mechanically-Recorded Lateral Frequency Records, 1958.....	1940
Correspondence:	
D-Day in Engineering Education, C. E. Hendrix and G. W. Hann.....	1947
Current Build-Up in Semiconductor Devices, W. Shockley and J. Gibbons.....	1947
On the Need for Revision in Transistor Terminology and Notation, H. L. Armstrong.....	1949
Antipodal Reception of Sputnik III, O. K. Garriott and O. G. Villard, Jr.....	1950
WWV Standard Frequency Transmissions, W. D. George.....	1950
Compound Interferometers, N. F. Barber, A. E. Covington, and N. W. Broten.....	1951
Potential Well Theory of Velocity Modulation, L. Gold.....	1952
Parallel Plane Waveguide Partially Filled with a Dielectric, M. Cohn.....	1953
An Effect of Pulse Type Radiation on Transistors Packaged in a Moist Atmosphere, W. A. Boham, M. G. Chasanov, and E. N. Schroeder.....	1953
Theory of the P-N Junction Device Using Avalanche Multiplication, T. Misawa.....	1954
Number of Trees in a Graph, L. Weinberg.....	1954
Algebraic Approach to Signal Flow Graphs, A. Nathan.....	1955
On the Coupling Coefficients in the "Coupled-Mode" Theory, A. Yariv.....	1956
Effect of Beam Coupling Coefficient on Broad-Band Operation of Multicavity Klystrons, S. V. Yadavalli.....	1957
Improvements in Some Bounds on Transient Responses, A. H. Zemanian.....	1958
Geometric-Analytic Theory of Noisy Two-Port Networks, E. F. Bulmer.....	1959
Comparison of Phase Difference and Doppler Shift Measurements for Studying Ionospheric Fine Structure Using Earth Satellites, M. C. Thompson, Jr. and D. M. Waters.....	1960
AM Transmitters As SSB Jammers, J. P. Costas.....	1960
Taper Sections in Circular Waveguides, G. Gerosa.....	1961
Common Emitter Transistor Amplifiers, R. F. Furton.....	1961
Resonance-Probability and Entropy-Evolution Relationships, G. H. Amber.....	1962
The Dependence of Minority Carrier Lifetime on Majority Carrier Density, D. M. Evans.....	1962
The Internal Current Gain of Drift Transistors, P. J. Hyde.....	1963
Theory of Diode and Transistor Noise, H. F. Mataré.....	1964
Dispersion of High-Frequency Elastic Waves in Thin Plates, D. L. Aronberg.....	1965
Computer Fabrication and Circuit Techniques, F. Herzfeld.....	1965
Radiometer Circuits, M. Graham.....	1966
Application of Inductive Probability to Communications, L. S. Schure.....	1966
A Transistor Magnetic Core Binary Counter, H. R. Irons.....	1967
Tropospheric Effects on 6-MC Pulses, R. Silberstein.....	1968
A New Type of Fading Observable on High-Frequency Radio Transmissions Propagated over Paths Crossing the Magnetic Equator, K. C. Yeh and O. G. Villard, Jr.....	1968
A Note Concerning Instantaneous Frequency, D. A. Linden.....	1970
Contributors.....	1971
Scanning the TRANSACTIONS.....	1972
Books:	
"Feedback Theory and Its Applications," by P. H. Hammond, Reviewed by J. E. Bertram.....	1973
"Space Charge Waves and Slow Electromagnetic Waves," by A. H. W. Beck, Reviewed by J. R. Pierce.....	1973
"English-Russian, Russian-English Electronics Dictionary," compiled by Department of the Army, Reviewed by P. E. Green, Jr.....	1974
"Magnetic Tape Recording," by H. G. M. Spratt, Reviewed by A. Meyerhoff and K. McIlwain.....	1974
"Television Engineering, Vol. IV: General Circuit Techniques," by S. W. Amos and D. C. Birkinshaw, Reviewed by E. T. Jaynes.....	1974
Recent Books.....	1975
Abstracts of IRE TRANSACTIONS.....	1975
Abstracts and References.....	1980
IRE News and Radio Notes.....	14A

INDEX TO AUTHORS

Listings are by month and page, and include authors of papers, authors of Correspondence items (indicated by letter C), and reviewers of books (indicated by letter B).

A

Aarons, J. Jan 325
Adler, R. (C) Jun 1300, (C) Oct 1756
Adler, R. B. Aug 1517
Aharoni, A. (C) Apr 780
Aisenstein, S. M. (C) Apr 780
Aiya, S. V. C. Mar 580, Aug 1502
Akabane, K. Jan 194
Albersheim, W. J. (B) Sep 1663
Albus, J. S. (C) Mar 610, (C) Aug 1534
Aldrich, R. W. Jun 1236
Amber, G. H. (C) Dec 1962
Ancker-Johnson, B. (C) Jul 1421
Anderson, J. R. Feb 441
Angell, J. B. Jun 1166
Angello, S. J. Jun 968
Anouchi, A. Y. (C) Mar 619
Arams, F. R. (C) May 912, 913
Arenberg, D. L. (C) Dec 1965
Armstrong, H. L. (C) Jan 361, (C) Jun 1307, (C) Aug 1541, (C) Dec 1949
Ashton, N. L. Jan 23
Atwood, W. L. (B) May 927
Autler, S. H. (C) Nov 1880
Avakian, A. (C) Apr 783
Axelby, G. S. (C) Aug 1549

B

Bachynski, M. P. Sep 1619
Baghdady, E. J. Feb 432, Apr 728
Baker, W. R. G. Mar 534
Barber, N. F. (C) Dec 1951
Bardeen, J. Jun 952
Barlow, H. M. Jul 1411, 1413
Barnes, F. S. (C) Jul 1427
Barrett, A. H. Jan 250
Barron, W. R. Jan 325
Batcher, R. R. (B) Mar 663
Bauer, B. B. (B) Jan 380, (B) Apr 794
Bean, B. R. (C) Jul 1425
Beattie, L. A. Apr 751
Beckmann, R. (C) Mar 617
Becking, A. G. T. Mar 589
Behrens, W. V. Mar 601
Beizer, B. (C) Apr 779
Bemski, G. Jun 990, Aug 1533
Bernstein, M. (C) Apr 782
Beutler, F. J. Oct 1758
Bingley, F. J. (B) May 928
Blackwell, W. A. (C) Jul 1428
Blecher, F. H. (B) Jul 1435
Bloom, S. Jul 1383
Blum, E. J. Jan 39
Bogner, B. F. Feb 498
Boham, W. A. (C) Dec 1953
Bolinder, E. F. (C) Sep 1650, (C) Dec 1959
Booker, H. G. Jan 298, Jun 1085
Bracewell, R. N. Jan 97, 106, 198, Apr 778
Brattain, W. H. Jun 953
Brennan, D. G. (C) Oct 1758
Brewer, G. R. Feb 441
Bridges, T. J. Feb 430, 494
Briggs, G. R. Nov 1808
Bronk, D. W. Jul 1352
Brotan, N. W. (C) Dec 1951
Brown, A. C. Apr 722
Brueckmann, H. Aug 1510
Bruton, R. H. Jan 293
Buchmiller, L. C. (C) Jul 1420
Burgener, R. C. Feb 476
Burr, R. P. (B) Mar 622
Bush, D. (C) Nov 1882
Busignies, H. (B) Jun 1323

C

Cacheris, J. C. Mar 594
Cagle, W. B. (B) Apr 796, (B) Aug 1548
Caicoya, J. I. (C) Apr 787
Campopiano, C. N. (C) Sep 1652
Cappuccini, F. (C) Apr 784
Caruso, F. (C) Nov 1875
Castelli, J. P. Jan 325
Cataldo, J. T. (B) Mar 663.

Caulton, M. (C) May 911
Champlin, K. S. (C) Apr 779
Chang, K. K. N. Jul 1383
Chapline, J. D. (B) Jul 1438
Chasanov, M. G. (C) Dec 1953
Chen, T. C. May 839
Chennette, E. R. (C) Jun 1304
Chipp, R. D. (B) Oct 1770
Chodorow, M. Feb 497
Chorney, P. (C) Jan 360
Christiansen, W. N. Jan 127
Clark, M. A. Jun 1185
Clarke, G. M. (C) May 914, (C) Sep 1652
Clarke, K. K. May 889
Clavier, P. A. (C) May 918
Coates, R. J. Jan 122
Cobine, J. D. (B) May 929
Coffey, W. N. Feb 495
Cohen, M. H. Jan 172, 183
Cohn, J. May 889
Cohn, M. (C) Dec 1953
Cole, R. S. Apr 722
Colin, L. (C) Jan 356
Combelic, D. (B) Nov 1886
Comerci, F. A. (B) Jun 1323
Conwell, E. M. Jun 1281
Cook, E. J. Feb 497
Coon, R. M. Dec 1914
Costas, J. P. Jul 1396, (C) Dec 1960
Coutrez, R. Jan 274
Covington, A. E. Jan 112, (C) Dec 1951
Craig, K. J. Jan 293
Cremošnik, G. May 868
Cripps, L. G. (C) Apr 781
Curnow, H. J. Feb 430
Currie, M. R. Mar 570, (C) May 911

D

Dacey, G. C. (B) Aug 1550
Dahlke, W. Sep 1639
Darlington, S. (B) Jul 1436
Dautremont, J. L., Jr. (C) Sep 1654
Davis, C. C. Oct 1686
Denisse, J. F. Jan 39
Deschamps, G. (B) Jul 1435
Develet, J. A., Jr. (C) Aug 1541
De Vito, G. (C) Mar 617
DeVore, L. T. (B) Jan 379, (B) Feb 509, (B) Apr 794
Dickson, F. H. Jul 1350
Dieter, N. H. Jan 234
Dinger, H. E. Jul 1366, 1401
Dion, D. F. (C) May 920
Dishal, M. Feb 498
Disman, M. I. May 895
Dlouhy, F. Sep 1639
Dodson, H. W. Jan 149
Drake, F. D. Jan 53
Drees, E. E. Sep 1580
Duncan, B. J. Feb 500

E

Early, J. M. Dec 1924
Eastman, A. V. (B) Jul 1437
Eckles, W. (C) May 910
Edson, W. A. May 895
Ellyett, C. Oct 1711
Embersen, R. M. Jan 23
Emeis, R. Jun 1216, 1220
Engelbrecht, R. S. (C) Sep 1655
Evans, D. M. (C) Dec 1962
Ewen, H. I. Jan 53

F

Fano, R. M. (B) Mar 662
Farris, H. W. (C) Nov 1876
Feucht, D. (C) Nov 1871
Field, G. B. Jan 240
Findlay, J. W. Jan 35
Fink, D. G. May 823
Finlay, W. H. (C) Jan 357
Fontana, J. R. (C) Jul 1424
Forrer, M. P. Nov 1830
Forster, D. C. Mar 570
Franklin, P. J. Oct 1723

Frayne, J. G. Oct 1686
Frei, A. May 868
Frei, E. H. (C) Apr 780

G

Gallagher, P. B. Jan 89
Garner, W. E. Jul 1401
Garriott, O. K. (C) Dec 1950
Gärtner, W. W. (C) Jul 1422, (C) Nov 1875
Gaskins, F. J. Nov 1798
Gasparini, F. (C) Apr 784
Gehrels, E. (C) Apr 785
George, W. D. (C) May 910, (C) Jun 1309, (C) Jul 1420, (C) Aug 1534, (C) Sep 1649, (C) Oct 1758, (C) Nov 1881, (C) Dec 1950
Geppert, D. V. (C) Sep 1658
Gerber, E. A. Oct 1731
Gerosa, G. (C) Dec 1961
Gershon, J. J. (B) Mar 664
Giacoletto, L. J. (B) Mar 664, Jun 1083
Gibbons, J. (C) Dec 1947
Gibson, J. E. Jan 280
Giguere, W. J. Apr 693
Giordano, A. B. (B) Feb 508, (B) May 928
Glass, M. S. Oct 1751
Gleichauf, P. H. (C) Aug 1542
Glicksman, R. Aug 1462
Gold, L. (C) Dec 1952
Goode, H. H. (B) Jun 1322
Goodman, J. Jan 132
Gordon, J. P. Sep 1588
Gordon, W. E. Nov 1824
Goudoulis, G. H. (C) Apr 782
Graf, C. R. (C) May 915
Graham, M. (C) Dec 1966
Green, J. H., Jr. Oct 1741
Green, P. E., Jr. Mar 555
Gremmelmaier, R. Jun 1045
Guillemin, E. A. (B) Jul 1437

H

Haddock, F. T. Jan 3, Jul 1373, (B) Aug 1546
Haines, A. B. (B) Oct 1771
Halpern, J. Jun 1068
Hamilton, D. H., Jr. Jul 1401
Hanel, R. (C) Nov 1875
Hann, G. W. (C) Dec 1947
Harrington, R. D. (C) Apr 784
Harris, L. A. (C) Mar 615, (C) Sep 1655
Hatsopoulos, G. N. Sep 1574
Haus, H. A. Aug 1517
Heschen, D. S. Jan 234
Heffner, H. (C) Jun 1301
Helbig, W. A. (C) Sep 1649
Helliwell, R. A. (C) Apr 785, (C) Oct 1760
Hellestrom, M. J. Feb 502
Henderson, K. W. Nov 1860
Hendricks, C. D., Jr. (C) Oct 1763
Hendrix, C. E. (C) Dec 1947
Henkels, H. W. Jun 1086
Henle, R. A. Jun 1240
Herbstreit, J. W. (C) Aug 1535
Herlet, A. Jun 1216, 1220
Herman, F. (B) Jan 379
Herold, E. W. (C) Jan 360, (C) May 914, (C) Nov 1879
Herrmann, G. F. (C) Jun 1301
Herzfeld, F. (C) Dec 1965
Herzog, G. B. (B) Sep 1663
Hey, J. S. Jan 119
Higgy, R. C. (C) Aug 1534
Hoadley, G. B. (B) Aug 1547
Hochstadt, H. (C) Sep 1652
Hoepfner, C. H. (B) Nov 1887
Hoerni, J. A. Feb 502
Holbrook, G. W. (C) Oct 1762
Holmes, D. D. Jun 1255
Holonyak, N. Jun 1236
Honeyman, W. N. Apr 722
Hopkin, A. M. (B) Feb 508
Houlding, N. (C) May 917
Hrbek, G. (C) Oct 1756

Hughes, V. A. Jan 119
Hulst, G. D. (C) Nov 1882
Hunaerts, J. Jan 274
Hyde, F. J. (C) Dec 1963

I

Irons, H. R. (C) Dec 1967
Iwersen, J. E. Jun 1207, 1209

J

Jaffe, D. Mar 594
Jaffe, H. (B) Oct 1769
James, J. C. (C) Nov 1871
Jansky, C. M., Jr. Jan 13
Jasik, H. Jan 135
Jaumot, F. E., Jr. Mar 538, Sep 1587
Jaynes, E. T. Feb 416, (B) Sep 1664
Jean, A. G. (C) Oct 1760
Jeanneney, J. P. (B) Jun 1324
Jenny, D. A. Apr 717, Jun 959, (B) Aug 1549
Jochems, P. J. W. Jun 1161
Johansen, D. May 827
Johnston, R. C. May 830
Jones, T. O. (C) May 917
Jordan, E. C. Jul 1376

K

Kahn, L. R. (C) Jul 1429
Karayianis, N. Mar 594
Karbowski, A. E. Oct 1706
Katzin, M. (B) Feb 509
Kaye, J. Sep 1574
Kennedy, R. C. Nov 1798
Kerns, D. M. (C) Nov 1881
Keywell, F. Jun 1209
Kinaman, E. W. May 861
King, B. G. (C) May 922
King, S. Feb 476
Kingston, R. H. (C) May 916
Kirstein, P. T. Oct 1716
Kita, S. (C) Jun 1307
Ko, H. C. Jan 208, (C) Nov 1872
Kock, W. E. Feb 499
Koeckelenbergh, A. Jan 274
Koenig, H. E. (C) Jul 1428
Koerner, L. F. Oct 1731
Kopaczek, T. F. (C) Aug 1537
Kosowski, D. I. Feb 419
Kotzebue, K. (C) June 1301
Koury, F. (B) Aug 1550
Kraus, J. D. Jan 92, 266, (C) Mar 610, (C) 611, (C) 612, (C) May 912, (C) Aug 1534, Sep 1580

L

Labus, J. (C) Jan 358
Lair, J. B. (B) Nov 1886
Lamb, J. J. (B) Jun 1324
Lampi, E. E. Aug 1483
Lawrence, R. S. Jan 315
Layden, O. P. (C) Apr 782
Lea, N. Nov 1835
Lebenbaum, M. Jan 132
Lees, G. B. (C) May 914
Leighton, H. Oct 1711
Leinbach, H. Jan 334
Leonides, C. T. (B) Apr 796
Levenstein, H. Feb 486
Lilley, A. E. Jan 221
Linden, D. A. (C) Dec 1970
Linville, J. G. Jun 1141
Lippel, B. (B) Oct 1771
Little, A. G. Jan 67
Little, C. G. Jan 334
Lo, A. W. Nov 1808
Locke, W. N. (B) Apr 797
Lorenz, C. S. (C) Sep 1651
Louisell, W. H. Apr 707
Lozier, G. S. Aug 1462
Lucke, W. H. (C) Nov 1877

M

Mackintosh, I. M. Jun 1229
Maeda, H. (C) Aug 1536
Magid, M. May 861
Manning, L. A. Jul 1362, (B) Sep 1662

Marshall, L. Jan 215
 Matare, H. F. (C) Dec 1964
 Mathewson, D. S. Jan 127
 Matraw, H. C. (B) Sep 1662
 Matz, A. W. (C) Mar 616
 Maxwell, A. Jan 142
 Maxwell, E. L. Dec 1914
 Mayer, C. H. Jan 260
 McClain, E. F. Jan 221
 McCoy, C. T. Jan 61
 McCullough, T. P. Jan 260
 McKenna, J. (C) May 922
 McWhorter, A. L. (C) May 913
 Medd, W. J. Jan 112
 Meek, T. J. Apr 692
 Meeks, M. L. (C) Nov 1871
 Memelink, O. W. Jun 1161
 Menon, T. K. Jan 230
 Mertz, P. (B) Jul 1438
 Messenger, G. C. Jun 1038, 1116
 Met, V. (C) Sep 1656
 Miessner, B. F. (C) Jul 1430
 Millman, G. H. Aug 1492
 Mills, B. Y. Jan 67
 Misawa, T. (C) Dec 1954
 Moll, J. L. Jun 1076, 1177, (C) 1306
 Montgomery, G. F. (C) Jul 1423
 Moody, R. C. (C) Apr 782
 Moore, A. R. May 929
 Morehouse, C. K. Aug 1462
 Morrow, R. E. (C) Jan 357
 Morton, J. A. Jun 955
 Mueller, R. E. (C) Apr 783

N

Nathan, A. (C) Dec 1955
 Nelson, H. Jun 1062
 Nelson, J. T. Jun 1207, 1209
 Neugebauer, H. E. J. Sep 1619
 Niklas, W. F. (C) Aug 1539
 Nitzberg, (C) Mar 614

O

Ogawa, T. Dec 1934
 O'Meara, T. R. Nov 1848
 Ording, P. F. (B) May 929
 Otley, K. O. Oct 1723
 Otterman, J. (C) Apr 781

P

Paanen, R. A. Feb 500
 Packard, K. S. (C) Jan 362
 Page, C. H. Oct 1738
 Page, D. F. Jun 1271
 Pankove, J. I. (B) Aug 1546
 Pankraz, O. (C) Sep 1653
 Pantell, R. H. Dec 1910
 Papoulis, A. (C) Jan 361, Mar 606, May 839
 Pawsey, D. C. (C) Oct 1763
 Penfield, H. Jan 321
 Pfister, W. (B) Apr 795
 Piddington, J. H. Jan 349
 Pierce, J. N. (C) May 903
 Pietenpol, W. J. Jun 955

Pineo, V. C. (C) May 922
 Plush, R. W. Dec 1914
 Poole, K. M. Jul 1387
 Powell, R. C. (C) Apr 784
 Powell, T. (C) Nov 1870
 Price, R. Mar 555
 Pritchard, R. L. Jun 1130, 1152
 Purl, O. T. Feb 441
 Purton, R. F. (C) Dec 1961

Q

Quate, C. F. Apr 707

R

Raisbeck, G. (C) May 922
 Rajchman, J. A. Nov 1808
 Ramsay, J. F. Feb 405
 Reber, G. Jan 15
 Rediker, R. H. Jun 1068, 1122
 Reich, B. Jun 1204
 Reiger, S. (C) May 919
 Richter, W. (B) Aug 1549
 Ridenour, L. N. (B) Sep 1663
 Rigrod, W. W. (C) Jan 358
 Roman, N. G. Jan 199, 293
 Rosenthal, J. E. (C) Jul 1422
 Rowe, H. E. May 850
 Rowley, J. J. (C) Jul 1421
 Rudenberg, H. G. (C) Jun 1304
 Rush, S. (C) Jan 356

S

Saby, J. S. (B) Oct 1769
 Sack, E. A. Oct 1694
 Salzberg, B. (C) Jun 1303, (C) Aug 1536
 Salzer, J. M. (B) Aug 1551
 San Soucie, R. L. Oct 1741
 Sard, E. W. (C) Jun 1303
 Sawyer, D. E. Jun 1122
 Schorn, R. A. (C) Oct 1763
 Schroeder, E. N. (C) Dec 1953
 Schultz, F. V. Feb 476
 Schwartz, J. W. Nov 1864
 Schwartz, L. S. (C) Dec 1966
 Schwartzman, A. (C) May 915
 Scott, W. T. (C) Apr 782
 Seki, H. Apr 758
 Sellers, B. Feb 498
 Senitzky, B. (C) Jun 1306
 Shain, C. A. Jan 85
 Shapiro, G. (B) Aug 1551
 Shaull, J. M. Mar 601
 Shaw, H. J. (C) Jul 1424
 Shepherd, W. G. Jul 1381
 Sheridan, K. V. Jan 67, 160
 Shockley, W. Jun 954, 973, (C) Dec 1947
 Shoemaker, R. F. Oct 1723
 Shtrikman, S. (C) Apr 780
 Siebert, W. M. (B) Aug 1547
 Siegel, K. (C) Aug 1536
 Silber, L. M. (C) Aug 1538
 Silberstein, R. (C) Dec 1968
 Slee, O. B. Jan 67
 Slepian, D. (C) Mar 614
 Sloanaker, R. M. Jan 260
 Smith, C. E. (B) Mar 662
 Smith-Rose, R. L. (C) Nov 1874
 Smits, F. M. Jun 1049
 Smullin, L. D. (C) Jan 360
 Smyth, J. B. Jul 1385
 Sobel, A. (C) Jul 1426
 Solyman, L. (C) Mar 618, (C) Apr 779
 Soohoo, E. L. (C) May 917
 Soohoo, R. F. (C) Apr 788
 Sparkes, J. J. (C) Jun 1305
 Spence, E. Jun 1220
 Spratt, J. P. Jun 1038
 Stableford, C. V. Jan 198
 Stahl, P. D. (C) May 915
 Stampf, R. (C) Nov 1875
 Stein, S. May 827
 Steinberg, J. L. Jan 39
 Stern, A. P. (B) Jun 1322
 Stewart, J. L. (C) Nov 1873
 Stewart, R. M. (C) Nov 1873
 St. John, G. E. (C) May 911
 Stockman, H. (C) Mar 615
 Stone, J. L. Feb 499
 Storer, J. E. (C) Sep 1649
 Stout, T. M. (B) Jul 1436, (B) Oct 1770
 Straiton, A. W. (B) Aug 1547
 Strum, P. D. Jan 43
 Strutt, M. J. O. May 868
 Stuart, R. W. (B) Nov 1887
 Suhl, H. Apr 700
 Suran, J. J. Jun 1260
 Suisskind, C. Feb 497
 Suzuki, S. Jan 190
 Swarup, G. Jan 142
 Swenson, G. W., Jr. (C) Oct 1763
 Swern, L. Feb 500
 Sydnor, R. L. Nov 1848
 Szentirmai, G. (C) Aug 1538
 Sziklai, G. C. (B) Mar 663

T

Tanzman, H. D. (C) Apr 782
 Taub, J. J. Feb 498
 Taylor, W. L. (C) Oct 1760
 Teachman, A. E. Jul 1401
 Thomas, D. E. Jun 1177
 Thompson, A. R. Jan 142
 Thompson, M. C., Jr. (C) Aug 1535, (C) Dec 1960
 Thornton, C. G. Jun 1166
 Tien, P. K. Apr 700, Jul 1387
 Toman, K. Feb 495
 Tomiyasu, K. Feb 500
 Tompkins, H. E. (B) Mar 662
 Tou, J. (C) May 915
 Tracy, R. A. (B) Jun 1323
 Treuhaft, M. A. (C) Aug 1538
 Trexler, J. H. Jan 286
 Tsuchiya, A. Jan 190
 Tummers, L. J. Jun 1161
 Turin, G. L. Sep 1603, (C) Oct 1757, Dec 1913

U

Uenohara, M. (C) Jun 1301
 Uhler, A., Jr. Jun 1099, (C) 1301, (C) 1306
 Unger, D. M. (C) Apr 783
 Unger, S. H. Oct 1744

V

van der Ziel, A. Mar 589, Jun 1019, (C) Jul 1426
 van Vliet, K. M. Jun 1004
 Van Voorhis, S. N. (B) May-927
 Villard, O. G., Jr. (C) Dec 1950, (C) Dec 1968
 von Aulock, W. H. (B) Apr 796

W

Wada, G. Oct 1700
 Wade, G. (C) Jul 1420, (C) Oct 1756
 Wait, J. R. (C) Aug 1539
 Walsh, D. (C) Jun 1309
 Walsh, J. L. Jun 1240
 Wang, F. B. (C) Sep 1657
 Warnick, A. (B) Jul 1437
 Warren, F. H. (C) Nov 1879
 Waterman, A. T., Jr. Nov 1842
 Waters, D. M. (C) Dec. 1960
 Watkins, D. A. Oct 1700
 Watt, A. D. Dec. 1914
 Watters, R. L. (C) Jul 1426
 Weber, E. Jul 1354, (B) Aug 1548
 Weinberg, L. Apr 739, Jun 1184, (C) Dec 1954
 Weiner, J. R. (B) Mar 664
 Wells, H. W. Jan 205, (C) Mar 610, Jul 1351
 Wheeler, H. A. Sep 1595
 Whirry, W. L. (C) Sep 1657
 White, L. D. Sep 1588
 White, W. D. (C) May 920, (B) Oct 1771
 Wiener, N. (C) Oct 1758
 Wild, J. P. Jan 160
 Wilson, R. D. (B) Jul 1436
 Wintringham, W. T. (B) Jun 1325
 Wong, M. S. Sep 1628
 Woodford, J. B., Jr. (C) Nov 1871
 Wouk, V. (B) May 927

Y

Yadavalli, S. V. (C) Dec 1957
 Yaplee, B. S. Jan 199, 293
 Yariv, A. (C) Dec 1956
 Yeh, K. C. (C) Dec 1968

Z

Zarwyn, B. (C) Jun 1308
 Zemanian, A. H. (C) May 916, (C) Dec 1958
 Zuleeg, R. (C) Nov 1878

INDEX TO SUBJECTS

Listings are by month and page. Authors and paper titles may be determined from the tables of contents in the front part of this index.

A

Absorption Techniques for 21-CM Astronomy Research: Jan 221
 Airborne Propagation, Refraction Anomalies in: Sep 1628
 Amplification, Parametric, of the Fast Electron Wave: Jun 1300
 Amplifiers:
 Ferromagnetic Microwave, Phase Dependence of: Sep 1657
 Klystron Power, 8-mm: Feb 430
 Linear, Optimum Noise Performance: Aug 1517
 Maser, Noise in: Sep 1588
 Maser, Without Nonreciprocal Elements: Nov 1880
 Operational, Improved: Mar 614
 Parametric Electron Beam: Feb 494, Jun 1300
 Parametric, Low-Noise Electron-Beam: Oct 1756
 Parametric Microwave Semiconductor Diode: Jun 1301

Parametric, Using Lower-Frequency Pumping: Jul 1383
 Reactance, Low-Noise Wide-Band: Jun 1303
 Reactance, Variable, Semiconductor Diode, Noise Figure Measurements on: Jun 1301
 Resonator as a 200-MC Power: Aug 1483
 Transistor, Common Emitter: May 920, Dec 1961
 Transistor, Measuring Noise Figures of: Mar 619
 Traveling-Wave Ferromagnetic: Apr 700
 Traveling-Wave, Low-Noise Nonlinear Reactance: Sep 1655
 Traveling-Wave, Very-Low-Noise: May 861
 Video, with Stringent Electrical and Mechanical Requirements: Aug 1541
 Amplitude Scintillation of Extraterrestrial Radio Waves at UHF: Nov 1872
 Analog Computers, Impedance Networks as: May 868

Analog Solution of Space-Charge Regions in Semiconductors: Jun 1083
 Analogs, Electromagnetic, for the Gravitational Fields in the Vicinity of a Satellite: May 920
 Analogs, Hyperbolic: Feb 502
 Analogs Using Varistors, Hyperbolic: Oct 1762
 Antennas:
 Array for Meteor Studies and Radio Astronomy at 13 Meters: Jan 89
 Beyond-Horizon, Efficiency of: Mar 617
 Directional HF, Suppression of Undesired Radiation of: Aug 1510
 Microwave, Techniques Before 1900: Feb 405
 Reactance Theorem for: Apr 779
 Scanning the Sun with: Jan 127
 for Solar Studies: Jan 135
 Spherical Coil as: Sep 1595
 Telescope, Large Aperture: Jan 92
 VLF Monopole, Earth Currents Near: Aug 1539
 Aperture Correction for Instrumentation Sys-

tems: Apr 781
Arc Prevention Using *P-N* Junction Reverse Transient: Jun 1308
Astronomy, Radio: See *Radio Astronomy*
Asynchronous Oscillations, Simultaneous, in Class-C Oscillators: May 895
Atmospheric Effects on VHF and UHF Propagation: Aug 1492
Atmospheric Noise Interference to Medium Wave Broadcasting: Aug 1502
Atmospheric Noise Interference to Short-Wave Broadcasting: Mar 580
Atmospheric and Thermal Noise, Radio Systems Performance in the Presence of: Dec 1914
Atmospherics, Undersea and Underground: Nov 1870
Audio Systems, Stereophonic, Simplification of: Jul 1426
Audio Terms, IRE Standards on: Dec 1928
Autocorrelation Functions, Differentiability of: Oct 1758
Avalanche Multiplication, *P-N* Junction Device Using: Dec 1954

I

Backward-Wave Preamplifiers, Low Noise Tunable, for Microwave Receivers: Mar 570
Balun Transformer, Very-Wide-Band, for VHF and UHF: Nov 1848
Batteries: Aug 1462
Beam Amplifier, Parametric: Feb 494, Jun 1300
Beam Coupling Coefficient, Effect on Klystron Operation: Dec 1957
Beam Position, Effect on Deflection in Slit Lenses: Mar 615
Beam, Space-Charge-Balanced, Charge Distribution: Feb 497
Beyond-Horizon Links, Efficiency of Large Antennas in: Mar 617
Binary Counter, Transistor Magnetic Core: Dec 1967
Binary Reception through Fading and Noise, Error Probabilities for: Sep 1603; Correction: Dec 1913
Boolean Algebra for Analysis of Switch Diode Circuits: Apr 779
Bridge Method of Measuring Noise in Low-Noise Devices: Apr 779
Broadcasting, Medium Wave, Atmospheric Noise Interference to: Aug 1502
Broadcasting, Short-Wave, Atmospheric Noise Interference to: Mar 580
Bunched Electron Current in a Velocity Modulated Beam: Aug 1536

C

Capacitance of Shielded Balanced-Pair Transmission Line, Formulas for: May 922
Capacitance in Transistors, Effective Collector: Nov 1878
Carrier Lifetime, Minority, Dependence on Majority Carrier Density: Dec 1962
Carrier Mobilities at Low Injection Levels: Feb 502
Carrier-to-Noise Statistics for Carrier and Interference Characteristics: May 889
Cassiopeia A Measurements between 18.5 MC and 107 MC: Jan 205
Cathode Test Utilizing Noise Measurements: Sep 1639
Cathodes, Field-Emission, Harmonic Generation at Microwave Frequencies Using: Jul 1424
Cayley-Klein Model of Three-Dimensional Hyperbolic Space: Sep 1650
Chroma-Key Composites in Modern Television: Nov 1798
Circuits and Radio Waves, Report on URSI Commission VI: Jul 1376
Climatology, Radio, First Meeting on: Jul 1425
Closed Loop Control Systems with Error Sampling: Nov 1873
Coaxial Line, Microwave Magnetic Field in: Feb 500
Co-Channel FM Signals, Alternative Detection of: Nov 1876
Code Groups, Optimum Finite: Sep 1649
Codification of Lagrangian Formulation: Jul 1428
Coil, Spherical, as an Inductor, Shield, or Antenna: Sept 1595
Coils, Low-Q, Ladder Network Design Using: Apr 739; Correction: Jun 1184
Coils, Toroidal, High-Frequency Magnetic Permeability Measurements Using: Apr 784
Collector Capacitance in Transistors, Effective: Nov 1878
Colombia, Survey of Radio and Electronics in: Apr 692

Comet 1956 h Emission from, on 600 MC: Jan 274
Communication Technique, Rake, for Multipath Channels: Mar 555
Communications Equipment, Application of Transistors in: Jun 1255
Composites, Electronic, in Modern Television: Nov 1798
Computer Fabrication and Circuit Techniques: Dec 1965
Computer Oriented Toward Spatial Problems: Oct 1744
Computers, Analog, Impedance Networks as: May 868
Computers, Application of Transistors to: Jun 1240
Conical Taper in Circular Waveguide, Design of: Mar 618
Contract Reports, Government, Maximum Utility in: Jan 360, Nov 1879
Control Systems, Closed Loop, with Error Sampling: Nov 1873
Cornell Radio Polarimeter: Jan 183
Correlation Effects on Combiner Diversity: Jan 362
Cosmic Background Radiation Distribution of: Jan 208
Cosmic Rays and Radio Noise, Production of: Jan 215
Cosmical Electrodynamics: Jan 349
Counter, Radiation, Semiconductor *P-N* Junction: Aug 1536
Counter, Transistor Magnetic Core Binary: Dec 1967
Coupling Coefficients in "Coupled-Mode" Theory: Dec 1956
Cryotron, Switching Time of: Apr 780
Cryotron Switching Time, Superconductive Transition Mixer and: Nov 1871
Crystals:
Filter, High-Frequency, Design: Feb 419
High-Frequency Quartz Filter: Mar 617
Microwave Receivers, Present and Future Capabilities of: Jan 61
Noise, Mixer: May 917
Piezoelectric, IRE Standards on: Apr 764
Current Amplification Versus Emitter Current and Junction Temperature: Nov 1875
Cygnus A Measurements between 18.5 and 107 MC: Jan 205

D

Data Transmission, Error Rates in: May 919
Decoder and Encoder of High Efficiency, Error Correcting: Oct 1741
Deflection in Slit Lenses, Effect of Beam Position on: Mar 615
Delay Lines, Electron Tube, Tungsten vs Copper: Feb 500
Delta Entities, Various Definitions of: Sep 1653
Demodulator FM, Requirements for Interference Rejection: Feb 432
Detection of Co-Channel FM Signals, Alternative: Nov 1876
Detector, Ferrite Microwave: Mar 594
Diffraction by Smooth Cylindrical Mountains: Sep 1619
Diffusion, Formation of Junction Structures by Solid-State: Jun 1049
Diffusion Lengths, Method for Measuring: Jun 1045
Diffusion Techniques, Preparation of Semiconductor Devices by Lapping and: Jun 1062
Diode and Transistor Noise: Dec 1964
Diodes:
Gallium Arsenide Microwave: Apr 717
Harmonic Generator Using Nonlinear Capacitance of Germanium: Jun 1307
Junction, Noise: Mar 589
Lumped Models of: Jun 1141
Microwave Mixer, New Concepts in: Jun 1116
Outdiffusion for Production of: Jun 1068
Semiconductor, Forward Characteristic of: Jan 361
Semiconductor, Forward Switching Transient in: Jul 1427
Semiconductor, in High-Frequency Communications: Jun 1099
Semiconductor, Microwave Parametric Amplifier Using: Jun 1301
Semiconductor, Noise Figure Measurements on Variable Reactance Amplifiers Using: Jun 1301
Silicon, Microwave Transients from Avalanche: Jun 1306
Space and Space Charge: May 918
Switch Circuits, Boolean Algebra for Analysis of: Apr 779

Thermoelectron Engine: Sep 1574
Discriminator, Balanced Frequency, Noise Output of: Mar 614
Disk System, Westrex Stereophonic: Oct 1686
Display, ELF Electroluminescent: Oct 1694
Display Panels, Transfluxor Controlled Electroluminescent: Nov 1808
Diversity Combiner, Correlation Effects on: Jan 362
Diversity Improvement in Frequency-Shift Keying, Theoretical: May 903
Doppler Equation for Satellite Measurements: May 915
Doppler Measurements, Satellite: Apr 782
Doppler Shift Measurements for Studying Ionospheric Structure Using Satellites: Dec 1960
Drift Transistors, Transient Response of: May 830
Dynamic Spectrum Analyzer for Solar Studies: Jan 132

E

Earth Currents Near a VLF Monopole Antenna: Aug 1539
Earth Geometry, A Theorem: Feb 495
Editorial Policies, IRE, Section Survey of: May 822
Education, Engineering, D-Day in: Dec 1947
Education of Scientists, Mass: Jul 1430
Elastic Waves in Thin Plates, Dispersion of High-Frequency: Dec 1965
Electrodes Required to Produce Given Field Distribution: Oct 1716
Electroluminescent Display, ELF: Oct 1694
Electroluminescent Display Panels, Transfluxor Controlled: Nov 1808
Electrolytic Tank Design of Electron Guns: Feb 497
Electron Beams:
Bunched Electron Current in a Velocity Modulated: Aug 1536
Parametric Amplifier: Feb 494, Jun 1300
Parametric Amplifier, Low-Noise: Oct 1756
Space-Charge Waves Along: Jan 358
Electron Density Profiles in Ionosphere During IGY: Nov 1874
Electron Guns:
Annular Geometry: Nov 1864
Electrolytic Tank Design of: Feb 497
Low-Noise, for Microwave Tubes: May 911
Space-Charge High-Transconductance: Aug 1542
Electron Optical Action of an Annular Aperture Lens: Sep 1655
Electron Tube Delay Lines, Thermal Properties for: Feb 500
Electronic Composites in Modern Television: Nov 1798
Electronics, Radio, Report on URSI Commission VII: Jul 1381
Electronics: What's Coming After the Missile Age: Mar 534
Electrons, Holes, and Traps: Jun 973
ELF Electroluminescent Display: Oct 1694
Encoder and Decoder of High Efficiency, Error Correcting: Oct 1741
Engineering Education, D-Day in: Dec 1947
Engineers, Re-Invention by Young: May 914
Entropy-Evolution Relationships: Dec 1962
Entropy of a Message Source: Sep 1652
Equator, Magnetic, New Type of Fading Observable on Paths Crossing the: Dec 1968
Equivalence, Space-Frequency: Feb 499
Error Correcting Encoder and Decoder of High Efficiency: Oct 1741
Error Probabilities for Binary Reception through Fading and Noise: Sep 1603; Correction: Dec 1913
Error Rates in Data Transmission: May 919
Error Sampling, Closed Loop Control Systems with: Nov 1873
Extragalactic 21-CM Studies: Jan 234
Extraterrestrial Radio Waves at UHF, Amplitude Scintillation of: Nov 1872

F

Fading and Noise, Error Probabilities for Binary Reception through: Sep 1603
Fading Observable on Paths Crossing the Magnetic Equator, New Type of: Dec 1968
Feedback Circuits, Delayed: Apr 758
Ferrites:
Application to Microwave Switches, Phasers, and Isolators: Apr 722
Microwave Detector: Mar 594
Reciprocal Phase Shifter, Magnetron Tuning Using: Nov 1882

Toroids to Eliminate External Magnets and Reduce Switching Power: Aug 1538
 Transversely Magnetized, Cutoff Phenomena in: Apr 788
 Ferromagnetic Amplifier, Traveling-Wave: Apr 700
 Ferromagnetic Microwave Amplifier, Phase Dependence of: Sep 1657
 Ferromagnetic Resonance Frequency Converter: Jul 1387
 Filters:
 Band-Pass, with Minimum Insertion Loss: Feb 498
 Crystal, High-Frequency Design: Feb 419
 Crystals, High-Frequency Quartz: Mar 617
 Designing Elliptic-Function, Nomographs for: Nov 1860
 Optimum, with Monotonic Response: Mar 606
 Tchebycheff Symmetrical, Dissipative Effects in: Oct 1763
 Focusing Magnet, TWT Leakage Flux Around: Oct 1751
 Focusing, Periodic, High Power: Feb 441
 Foreign Articles, Translation of: May 917
 Frequency Converter, Ferromagnetic Resonance: Jul 1387
 Frequency Discriminator, Balanced, Noise Output of: Mar 614
 Frequency, Instantaneous: Dec 1970
 Frequency Modulation:
 Demodulator Requirements for Interference Rejection: Feb 432
 Receiver, Transistorized 150-MC: Apr 693
 Reception, Stronger-Signal Capture in: Apr 728
 Signals, Co-Channel, Alternative Detection of: Nov 1876
 Frequency-Shift Keying, Theoretical Diversity Improvement in: May 903
 Frequency-Space Equivalence: Feb 499
 Frequency Transmission, WWV Standard: May 910, Jun 1309, Jul 1420, Aug 1534, Sep 1649, Oct 1758, Nov 1881, Dec 1950
 Frequency Variations in Short-Wave Propagation: Dec 1934

G

Gallium Arsenide Microwave Diode: Apr 717
 Gamma Rays, Irradiation of P-N Junctions with: Jun 1045
 Garnets, Mixed, for Nonreciprocal Devices at Low Microwave Frequencies: Jul 1421
 Generator, Harmonic, Using Nonlinear Capacitance of Germanium Diode: Jun 1307
 Germanium N-P-I-N Junction Transistor Triodes: Apr 783
 Germanium and Silicon, Properties of: Jun 1281
 Germanium and Silicon Rectifiers: Jun 1086
 Ghost Modes in Imperfect Waveguides: Feb 416
 Government Contract Reports, Maximum Utility in: Jan 360, Nov 1879
 Graph, Number of Trees in: Dec 1954
 Gravitational Fields in the Vicinity of a Satellite, Electromagnetic Analogs for: May 920
 Grid High-Transconductance Guns, Space-Charge: Aug 1542

H

Hall Effect and Its Application to Microwave Power Measurement: Jul 1411
 Harmonic Generation with Ideal Rectifiers: Oct 1738
 Harmonic Generation at Microwave Frequencies Using Field-Emission Cathodes: Jul 1424
 Harmonic Generator Using Nonlinear Capacitance of Germanium Diode: Jun 1307
 Helitron Oscillator: Oct 1700
 History of Some Foundations of Modern Radio-Electronic Technology: Apr 780
 Holes, Electrons, and Traps: Jun 973
 Hydrogen Study of Stellar Associations and Clusters: Jan 230
 Hydrogen 21-CM Line, Excitation of: Jan 240
 Hyperbolic Analogs: Feb 502
 Hyperbolic Analogs Using Varistors: Oct 1762

I

Index to IRE Standards on Terms: Feb 449
 Inductive Probability, Application of: Dec 1966
 Inductor, Shield, or Antenna, Spherical Coil as: Sep 1595
 Information Theory Terms, IRE Standards on: Sep 1646

Instantaneous Frequency: Dec 1970
 Institute of Radio Engineers Editorial Policies, Section Survey of: May 822
 Instrumentation Systems, Aperture Correction for: Apr 781
 Interference:
 Atmospheric Noise, to Medium Wave Broadcasting: Aug 1502
 Atmospheric Noise, to Short-Wave Broadcasting: Mar 580
 Carrier-to-Noise Statistics for: May 889
 Output of Television Receivers, IRE Standards on Measurement of: Jul 1418
 Rejection, FM Requirements for: Feb 432
 Interferometer, Phase Tracking: Jan 321
 Interferometer for Solar Radiation: Jan 160
 Interferometers, Compound: Dec 1951
 Interferometry of Discrete Celestial Sources: Jan 106; Correction: Apr 778
 International Geophysical Year, Electron Density Profiles in Ionosphere During: Nov 1874
 International Scientific Radio Union:
 Address of Welcome: Jul 1352
 Circuits and Radio Waves, Report on Commission VI: Jul 1376
 Electronics, Radio, Report on Commission VII: Jul 1381
 Ionospheric Radio Propagation, Report on Commission III: Jul 1362
 Measurement Methods and Standards, Radio, Report on Commission I: Jul 1354
 Noise of Terrestrial Origin, Radio, Report on Commission IV: Jul 1366
 Radio Astronomy, Report on Commission V: Jul 1373
 Tropospheric Radio Propagation, Report on Commission II: Jul 1358
 Twelfth General Assembly of: Jul 1350
 What Is URSI: Jul 1351
 Invention and Insight: Apr 783
 Ion Columns, Reflections from Satellite-Produced: Oct 1763
 Ion Filled Waveguides: Jan 360
 Ionization, Field-Aligned Astronomical Observations in Presence of: Jan 356
 Ionosphere:
 Absorption Measurements Using Extraterrestrial Radio Waves: Jan 334
 Electron Density Profiles During IGY: Nov 1874
 Fine Structure Study Using Satellites: Dec 1960
 Perturbations of Radio Waves Penetrating: Jan 315
 Propagation, Report of URSI Commission III: Jul 1362
 Radio Stars to Study Refraction in: Jan 295; Correction: Jun 1085
 Solar Cycle Influence on VHF Scatter: Oct 1711
 Isolators, Microwave, Applications of Ferrites to: Apr 722

J

Jammers, SSB, AM Transmitter as: Dec 1960
 Joint Technical Advisory Committee—Ten Years of Service: May 823
 Junctions:
 Between Semiconductors Having Different Energy Gaps: Jun 1307
 P-N Device Using Avalanche Multiplication: Dec 1954
 P-N, Irradiation with Gamma Rays: Jun 1045
 P-N, Reverse Transient Arc Prevention Using: Jun 1308
 P-N, Theory for the Voltage-Current Characteristic of: Jun 1076
 Structures by Solid-State Diffusion, Formation of: Jun 1049
 Transistors, Noise Figure Behavior in: Feb 495

K

Keep-Alive Design for TR Tubes, Improved: Jun 1309
 Kinescope Gun, Annular Geometry: Nov 1864
 Klystron, Power Amplifiers, 8-MM: Feb 430
 Klystrons, Multicavity, Effect of Beam Coupling Coefficient on Operation: Dec 1957

L

Ladder Network Design Using Low-Q Coils: Apr 739; Correction: Jun 1184
 Ladder Networks, A Property of: May 916
 Lagrangian Formulation, Codification of: Jul 1428

Laplace Transforms, Series Expansion Method for Finding: Nov 1877
 Lapping and Diffusion Techniques, Preparation of Semiconductor Devices by: Jun 1062
 Launching IGY Satellites: Jan 357
 Leakage Flux Around a TWT Focusing Magnet: Oct 1751
 Lens, Annular Aperture, Electron Optical Action of: Sep 1655
 Lenses, Slit, Effect of Beam Position on Deflection in: Mar 615
 Lightning Enhancement of VHF Tropospheric Scatter Signal: May 915
 Lightning Impulses which Produce Whistlers: Oct 1760
 Longitudinal Propagation, Astronomical Observations, Effects on: Jan 356
 Luminance Signal Levels, Measurement of: Feb 482; Correction: Jul 1417
 Lunar Radio Echoes: Jan 286
 Lunar Thermal Radiation at 35 KMC: Jan 280

M

Magnet, TWT Focusing, Leakage Flux Around: Oct 1751
 Magnetic Core Binary Counter, Transistor: Dec 1967
 Magnetic Cores, Terminal Properties of: May 839
 Magnetic Equator, New Type of Fading Observable on Paths Crossing the: Dec 1968
 Magnetic Field, Microwave, in Coaxial Line: Feb 500
 Magnetic Permeability Measurements, High-Frequency, Using Toroidal Coils: Apr 784
 Magneto-Ionic Duct Propagation Using VLF Signals: Apr 785
 Magnetron Tuning Using a Ferrite Reciprocal Phase Shifter: Nov 1882
 Man, Radar Cross Section of: Feb 476
 Masers:

 Amplifiers, Noise in: Sep 1588
 Amplifiers Without Nonreciprocal Elements: Nov 1880
 Circular Systems, Design: May 912
 Solid-State, System-Noise Measurement of: May 913
 Solid-State UHF: May 916
 Measurement Methods and Standards, Radio, Report on URSI Commission I: Jul 1354
 Measurement of the Parameters of Piezoelectric Vibrators: Oct 1731
 Measuring Noise Figures of Transistor Amplifiers: Mar 619
 Message Source, Entropy of: Sep 1652
 Meteor-Burst Communication, Choice of Frequencies for: Nov 1871
 Meteor-Burst Communication Systems, Storage Capacity in: Sep 1649
 Meteor-Burst Communication, Transmission Error Function for: Jul 1423
 Meteor Studies at 13 Meters, Antenna Array for: Jan 89
 Meudon Observatory, Radio Astronomy at: Jan 39
 Micro-Alloy Diffused Transistors: Jun 1166
 Microwave Antenna and Waveguide Techniques Before 1900: Feb 405
 Milky Way Sources at 440 MC: Jan 199
 Millimicrosecond RF Pulse Transmission: Nov 1830
 Minimum Energy Triggering Signals: Apr 751
 Minimum Triggering Signals: Sep 1654
 Missile Age, What's Coming After the: Mar 534
 Mixers:

 Crystal Noise: May 917
 Diodes, Microwave, New Concepts in: Jun 1116
 Superconductive Transition, and Cryotron Switching Time: Nov 1871
 Tubes, Noise in: Jul 1426
 Mobile Single-Sideband Equipment: Jan 357
 Mode Theory, Coupling Coefficients in: Dec 1956
 Modes, Ghost, in Imperfect Waveguides: Feb 416
 Modulation, Pulse, Transmitted through a Linearly Modulated Transit-Time Device: Sep 1656
 Modulation, Velocity, Potential-Well Theory: Dec 1952
 Monotonic Response, Optimum Filters with: Mar 606
 Moon, Radar Echoes from: Jan 293
 Moon Radio Echoes: Jan 286
 Moon Thermal Radiation at 35 KMC: Jan 280
 Mountains, Smooth Cylindrical, Diffraction by: Sep 1619

Multipath Channels, Rake Communication Technique for: Mar 553, Nov 1882
Multivibrators, Transistor Monostable, for Pulse Generation: Jun 1260

N

National Radio Astronomy Observatory, Noise Levels at: Jan 35
National Radio Astronomy Observatory Radio Telescope: Jan 23

Networks:

Dissipationless, Theorem for: Aug 1538
of Fixed and Variable Resistors: Aug 1541
Impedance, as Analog Computers: May 868
Ladder, A Property of: May 916
Ladder, Using Low-Q Coils: Apr 739; Correction: Jun 1184
of Linearly Variable Resistances: Feb 486
Noisy Two-Port, Geometric-Analytic Theory of: Dec 1959
Theorem on Rectification: Mar 615
Neutron, Effects of Irradiation on Germanium and Silicon: Jun 1038
Neutron Radiation on Semiconductor Devices, Effects of: Mar 601

Noise:

Atmospheric Interference to Medium Wave Broadcasting: Aug 1502
Atmospheric Interference to Short-Wave Broadcasting: Mar 580
Error Probabilities for Binary Reception through: Sep 1603; Correction: Dec 1913
Figure, Behavior in Junction Transistors: Feb 495
Figure Measurements on Variable Reactance Amplifiers Using Semiconductor Diodes: Jun 1301
Figures of Transistor Amplifiers, Measuring: Mar 619
Junction Transistor and Diode: Mar 589
in Junction Transistors: Jun 1019
Levels at the National Radio Astronomy Observatory: Jan 35
in Low-Noise Devices, Bridge Method of Measuring: Apr 779
Low, Tunable Preamplifiers for Microwave Receivers: Mar 570
in Maser Amplifiers: Sep 1588
Measurements, Cathode Test Utilizing: Sep 1639
Mixer Crystal: May 917
in Mixer Tubes: Jul 1426
Output of Balanced Frequency Discriminator: Mar 614
Performance of Linear Amplifiers, Optimum: Aug 1517
Radar, Improvement of Range Determination with: Sep 1652; Oct 1757
in Semiconductors and Photoconductors: Jun 1004
Sources in Transistors, Flicker: Jun 1304
Terrestrial, Report of URSI Commission IV: Jul 1366
Thermal and Atmospheric, Radio Systems Performance in: Dec 1914
Nomograph for Designing Elliptic-Function Filters: Nov 1860
Nonlinear Capacitance of Germanium Diode, Harmonic Generator Using: Jun 1307
Nonlinear Element, Sampled-Data Systems Containing: May 915
Nonlinear Elements, Small Signal Theory, General Properties of: May 850
Nonlinear Reactance Traveling-Wave Amplifier, Low-Noise: Sep 1655
Nonlinear Resistive Elements, Power Relationships for: Dec 1910
Nonreciprocal Devices at Low Microwave Frequencies, Mixer Garnets for: Jul 1421

O

Observatory, Meudon, Radio Astronomy at: Jan 39
Observatory, National Radio Astronomy, Noise Levels at: Jan 35
Observatory, National Radio Astronomy Telescope Program: Jan 23
On the Earth Geometry—A Theorem: Feb 495
Operational Amplifier, an Improved: Mar 614
Optimum Filters with Monotonic Response: Mar 606
Optimum Finite Code Groups: Sep 1649
Optimum Noise Performance of Linear Amplifiers: Aug 1517

Oscillators:

Class-C, Simultaneous Asynchronous Oscillations in: May 895

Helitron: Oct 1700
Quartz Servo: Nov 1835
Transistor Circuits, Design: Jun 1271

P

Parametric Amplifiers:

Amplification of Fast Electron Wave: Jun 1300
Amplification of Space Charge Waves: Apr 707
Electron Beam: Feb 494
Low-Noise Electron-Beam: Oct 1756
Traveling-Wave Ferromagnetic: Apr 700
Using Lower-Frequency Pumping: Jul 1383
Using a Semiconductor Diode, Microwave: Jun 1301
Passive Repeater Using Double Flat Reflectors: Apr 784
Permeability Measurements, High-Frequency Magnetic, Using Toroidal Coils: Apr 784
Phase Dependence of a Ferromagnetic Microwave Amplifier: Sep 1657
Phase Difference Measurements of Satellites, Continuous: Aug 1535
Phase Shifter, Ferrite Reciprocal, Magnetron Tuning Using: Nov 1882
Phase Tracking Interferometer: Jan 321
Phasers, Microwave, Applications of Ferrites to: Apr 722
Photoconductors, Noise in Semiconductors and: Jun 1004
Photodiodes, Narrow Base Germanium: Jun 1122
Picture Tubes, Cutoff Voltage Characteristics of: Aug 1539
Piezoelectric Crystals, IRE Standards on: Apr 764
Piezoelectric Vibrators, Measurement of the Parameters of: Oct 1731
Planetary Radiation Measurements at CM Wavelengths: Jan 260
Planetary and Solar Emission at 11 Meters Wavelengths: Jan 266
Polarimeter, Cornell Radio: Jan 183
Polarimeter in Microwave Region: Jan 194
Polarimeter at 200 MC: Jan 190
Polarization Measurements, Radio Astronomy: Jan 172
Poles and Zeros Squared: Jan 361
Potential-Well Theory of Velocity Modulation: Dec 1952
Power Measurement, Microwave, Hall Effect and Its Application to: Jul 1411
Power Relationships for Nonlinear Resistive Elements: Dec 1910
Power Supplies, Transistor Regulated: Aug 1537
Power Transistors: Jun 1185
Preamplifiers, Low Noise Tunable, for Microwave Receivers: Mar 570
President Smiles: May 910
Probability, Inductive, Application of: Dec 1966
Probability-Resonance Relationships: Dec 1962
Pulse Generation, Transistor Monostable Multivibrators for: Jun 1260
Pulse Modulation Transmitted through a Linearly Modulated Transit-Time Device: Sep 1656
Pulse Trains, Random, Statistical Description of Coincidences Among: May 827
Pulse Transmission, Millimicrosecond RF: Nov 1830
Pumping to Extend Traveling-Wave-Tube Frequency Range: Jul 1420

Q

Quartz Filter Crystals, High-Frequency: Mar 617
Quartz Servo Oscillator: Nov 1835

R

Radar:

Cross Section of a Man: Feb 476
Echoes from the Moon: Jan 293
Noise, Improvement of Range Determination with: Sep 1652, Oct 1757
Space Exploration by: Nov 1824
Radiation Counter, Semiconductor P-N Junction: Aug 1536
Radiation of Directional HF Antennas and Transmission Lines, Suppression of Undesired: Aug 1510
Radiation, Neutron, Effects on Semiconductor Devices: Mar 601
Radiation, Pulse Type, Effect on Transistors Packaged in a Moist Atmosphere: Dec 1953

Radio Astronomy:

Absorption Techniques for 21-CM Research: Jan 221
Antenna System for Solar Studies: Jan 135
Cassiopeia A and Cygnus A Measurements: Jan 205
Comet 1956 h on 600 MC: Jan 274
Considerations in High-Sensitivity Radiometry: Jan 43
Cornell Radio Polarimeter: Jan 183
Cosmic Background Radiation: Jan 208
Cosmic Rays and Radio Noise, Production of: Jan 215
Cosmical Electrodynamics: Jan 349
Dynamic Spectrum Analyzer for Solar Studies: Jan 132
Early Experiments: Jan 15
Effects Due to Longitudinal Propagation: Jan 356
Extragalactic 21-CM Studies: Jan 234
High Resolution Radio Telescope for Use at 3.5 M: Jan 67
Hydrogen Study of Stellar Associations and Clusters: Jan 230
Hydrogen 21-CM Line, Excitation of: Jan 240
Interferometer for Solar Radiation: Jan 160
Interferometry of Discrete Celestial Sources: Jan 97; Correction: Apr 778
Introduction to: Jan 3
Ionospheric Absorption Measurements: Jan 334
Irregular Refraction in the Ionosphere: Jan 298; Correction: Jun 1085
Jansky's Discovery: Jan 13
Large Aperture Telescope Antennas: Jan 92
Lunar Radio Echoes: Jan 286
Lunar Thermal Radiation at 35 KMC: Jan 280
Measurements of Planetary Radiation: Jan 260
Measurements at VHF and Microwaves: Jan 325
Meteor Studies at 13 Meters, Antenna Array for: Jan 89
Meudon Observatory: Jan 39
Milky Way at 440 MC: Jan 199
Phase Tracking Interferometer: Jan 321
Perturbations of Radio Waves Penetrating the Ionosphere: Jan 315
Planetary and Solar Emission: Jan 266
Polarimeter in Microwave Region: Jan 194
Polarimeter at 200 MC: Jan 190
Polarization Measurements: Jan 172
Present and Future Capabilities of Microwave Crystal Receivers: Jan 61
Radar Echoes from the Moon: Jan 293
Radiometer, Source Comparison: Jan 53
Radiometers, Method of Calibrating: Jan 119
Report on URSI Commission V: Jul 1373
Restoration of Cosmic Noise Distribution in the Presence of Errors: Jan 106; Correction: Apr 778
Scanning the Sun with Antenna Array: Jan 127
Solar Activity Radio Spectrum: Jan 142
Solar Corona Characteristics: Jan 198
Solar Flares Study: Jan 149
Solar Flux Measurements at 10.7-CM: Jan 112
Solar Radiation at 4.3-MM: Jan 122
Spectral Lines in: Jan 250
Sydney 19.7-MC Radio Telescope: Jan 85
U. S. National Observatory, Noise Levels at: Jan 35
U. S. National Observatory Telescope Program: Jan 23
Radio Climatology, First Meeting on: Jul 1425
Radio Telescope:
Antennas of Large Aperture: Jan 92
High Resolution, for Use at 3.5 M: Jan 67
National Radio Astronomy Observatory: Jan 23
Sydney 19.7-MC: Jan 85
Radiometer Circuits: Dec 1966
Radiometers, High-Sensitivity Microwave, Considerations in: Jan 43
Radiometers, Method of Calibrating: Jan 119
Radiometers, Source Comparison, for Radio Astronomy: Jan 53
Rake Communication Technique for Multipath Channels: Mar 555, Nov 1882
Reactance Amplifier, Low-Noise Wide-Band: Jun 1303

Reactance Theorem for Antennas: Apr 779
Receivers:

Microwave Crystal, Present and Future Capabilities of: Jan 61
Microwave, Low Noise Tunable Preamplifiers for: Mar 570
Television, IRE Standards on Measurement of Interference Output of: Jul 1418
Transistorized 150-MC FM: Apr 693
Recombination in Semiconductors: Jun 990; Correction: Aug 1533
Records, Calibrating Mechanically-Recorded Lateral Frequency, IRE Standards on: Dec 1940
Rectification, Network Theorem on: Mar 615
Rectifiers, Germanium and Silicon: Jun 1086
Rectifiers, Harmonic Generation with Ideal: Oct 1738
Reflection, CW, Detection of Sputniks I and II by: Mar 611
Reflections from Satellite-Produced Ion Columns: Oct 1763
Reflectors, Double Flat, Passive Repeater Using: Apr 784
Refraction Anomalies in Airborne Propagation: Sep 1628
Refraction, Radio Stars to Study: Jan 298; Correction: Jun 1085
Re-Invention by Young Engineers: May 914
Repeater, Passive, Using Double Flat Reflectors: Apr 784
Reports, Government Contract, Maximum Utility in: Jan 360, Nov 1879
Research, Utility of Government Contract Reports: Jan 360, Nov 1879
Resistance, Transistor Thermal, Measurement of: Jun 1204
Resistive Elements, Nonlinear, Power Relationships for: Dec 1910
Resonator as a 200-MC Power Amplifier: Aug 1483
Resonance-Probability Relationships: Dec 1962
Restoration of Cosmic Noise Distribution: Jan 106; Correction: Apr 778
Root Loci, Properties of: Sep 1651

S

Sampled-Data Systems Containing Nonlinear Element: May 915

Satellites:

Antipodal Reception of Sputnik III: Dec 1950
Continuous Phase Difference Measurements of: Aug 1535
Doppler Measurements: Apr 782
Electromagnetic Analogs for Gravitational Fields in Vicinity of: May 920
Explorers I and III, Observations by CW Reflection: Aug 1534
Ion Columns, Reflections from: Oct 1763
Launching IGY: Jan 357
Measurements, Doppler Equation for: May 915
Phase Difference and Doppler Shift Measurements for Studying Ionospheric Structure Using: Dec 1960
Sputnik I's Last Days in Orbit: Sep 1580
USSR, Detection by CW Reflection: Mar 611
USSR, Last Days of: Mar 612
USSR, Signal Characteristics of: Mar 610
USSR, Unusual Propagation at 40 MC from: Mar 610
Scatter Signal, VHF Tropospheric, Lightning Enhancement of: May 915
Scatter, VHF Forward, Solar Cycle Influence on Lower Ionosphere and: Oct 1711
Scattering, Incoherent, by Free Electrons: Nov 1824
Scattering Relationships in Transhorizon Propagation: Nov 1842
Scientists, Mass Education of: Jul 1430
Section Survey of IRE Editorial Policies: May 822
Semiconductors:
Analog Solution of Space-Charge Regions in: Jun 1083
Compound, Transistor Research: Jun 959
Devices, Current Build-Up in: Dec 1947
Devices, Effects of Neutron Radiation on: Mar 601
Devices, Lapping and Diffusion Techniques: Jun 1062
Devices, Review of Other: Jun 968
Diffusion Problems, Impedance Networks for Solving: May 868
Having Different Energy Gaps, Junctions Between: Jun 1307
and Photoconductors, Noise in: Jun 1004

P-N Junction Radiation Counter: Aug 1536

Recombination in: Jun 990; Correction: Aug 1533

Servo Oscillator, Quartz: Nov 1835
Shield, Inductor, or Antenna, Spherical Coil as: Sep 1595
Short-Wave Broadcasting, Atmospheric Noise Interference to: Mar 580
Signal Characteristics of Sputnik I: Mar 610
Signal Flow Graphs, Algebraic Approach to: Dec 1955
Signal Levels, Television, Measurement: Feb 482; Correction: Jul 1417
Silicon:

Diodes, Microwave Transients from Avalanche-lanching: Jun 1306
and Germanium, Properties of: Jun 1281
and Germanium Rectifiers: Jun 1086
P-N-P-N Triodes, Electrical Characteristics of: Jun 1229
Power Transistors, Blocking Capability of Alloyed: Jun 1216
Single-Sideband Jammers, AM Transmitters as: Dec 1960
Single-Sideband Mobile Equipment: Jan 357
Single-Sideband System, Kahn Compatible, Mathematical Analysis of: Jul 1396; Comment on: Jul 1429
Slotted Line, Tuning a Probe in: Apr 787
Solar:

Activity, Radio Spectrum of: Jan 142
Corona Characteristics: Jan 198
Cycle Influence on Lower Ionosphere and VHF Scatter: Oct 1711
Flares Study: Jan 149
Noise Studies, Antenna for: Jan 135
Planetary Emission at 11 Meters Wavelength: Jan 266
Radiation at 4.3 MM: Jan 122
Radiation, Interferometer for: Jan 160
Radio Flux Measurements at 10.7-CM: Jan 112
Studies, Dynamic Spectrum Analyzer for: Jan 132

Solenoid Systems, Minimum Weight: Sep 1652
Solenoids, Foil, Leakage in: May 914
Space Charge:

Balanced Beam Charge Distribution: Feb 497
Diffusion Problems, Impedance Networks for Solving: May 868
Grid High-Transconductance Guns: Aug 1542
Regions in Semiconductors, Analog Solution of: Jun 1083
Waves Along Electron Beams: Jan 358
Waves, Parametric Amplification of: Apr 707

Space Exploration by Radar: Nov 1824
Space-Frequency Equivalence: Feb 499
Spectral Analysis: Apr 782
Spectral Lines in Radio Astronomy: Jan 250
Spherical Coil as an Inductor, Shield, or Antenna: Sep 1595

Sputnik:

I, Last Days of: Mar 612
I's Last Days in Orbit: Sep 1580
I, Signal Characteristics of: Mar 610
I and II, Detection by CW Reflection: Mar 611
III, Antipodal Reception of: Dec 1950
USSR, Unusual Propagation at 40 MC from: Mar 610

Standards:

Audio Terms, IRE: Dec 1928
Calibrating Mechanically-Recorded Lateral Frequency Records, IRE: Dec 1940
Index to IRE Definitions of Terms, 1942-1957: Feb 449
Information Theory Terms, IRE: Sep 1646
Piezoelectric Crystals, IRE: Apr 764
Radio Measurement Methods and, Report on URSI Commission I: Jul 1354
Television, Measurement of Luminance Signal Level, IRE: Feb 482
Television Receivers, Measurement of Interference Output, IRE: Jul 1418
Testing Point-Contact Transistors, IRE: May 878

Statistical Description of Coincidences Among Random Pulse Trains: May 827
Statistics of Filled Vessels: Nov 1873
Stereophonic Audio Systems, Simplification of: Jul 1426
Stereophonic Disk System, Westrex: Oct 1686
Storage Capacity in Meteor-Burst Communication Systems: Sep 1649

Stronger-Signal Capture in FM Reception: Apr 728

Submillimetric Region, Guided Wave Propagation in: Oct 1706
Sun, Scanning with Antenna Array: Jan 127
Superconductive Transition Mixer and Cryotron Switching Time: Nov 1871
Surface Waves: Jul 1413
Switches:

Diode Circuits, Boolean Algebra for Analysis of: Apr 779
Microwave, Applications of Ferrites to: Apr 722
Multiterminal P-N-P-N: Jun 1236
Voltage Sensitive: Oct 1723
Switching Time, Cryotron, Superconductive Transition Mixer and: Nov 1871
Switching Time of Cryotron: Apr 780

T

Taper Sections in Circular Waveguides: Dec 1961

Tchebycheff Symmetrical Filters, Dissipative Effects in: Oct 1763

Telescope: See *Radio Telescope*

Television:

Modern, Electronic Composites in: Nov 1798
Picture Tubes, Cutoff Voltage Characteristics of: Aug 1539
Receivers, Standards on Measurement of Interference Output of: Jul 1418
Standards, on Luminance Signal Levels: Feb 482; Correction: Jul 1417

Temperature Rise of Transistors, Measurement of Internal: Jun 1207

Thermal and Atmospheric Noise, Radio Systems Performance in: Dec 1914

Thermal Resistance in Junction Transistors: Jun 1305

Thermal Resistance, Transistor, Measurement of: Jun 1204

Thermoelectric Effects: Mar 538

Thermoelectron Engine, Diode Configuration of: Sep 1574

Three-Dimensional Hyperbolic Space, Cayley-Klein Model of: Sep 1650

Toroids, Ferrite, to Eliminate External Magnets and Reduce Switching Power: Aug 1533

Transfluxor Controlled Electroluminescent Display Panels: Nov 1808

Transformer, Very-Wide-Band Balun, for VHF and UHF: Nov 1848

Transforms, Laplace, Series Expansion Method for Finding: Nov 1877

Transhorizon Propagation, Scattering Relationships in: Nov 1842

Transient, Forward Switching, in Semiconductor Diodes: Jul 1427

Transient Response of Drift Transistors: May 830

Transient Responses, Improvements in Some Bounds on: Dec 1958

Transients from Avalanche Silicon Diodes: Microwave: Jun 1306

Transistors:

Alloyed Silicon Power, Blocking Capability of: Jun 1216
Amplifiers, Common Emitter: May 920
Dec 1961
Amplifiers, Measuring Noise Figures of: Mar 619
Applications in Communications Equipment: Jun 1255
Applications to Computers: Jun 1240
Business, Invited Essay on: Jun 954
Correlation Between Flicker Noise Source in: Jun 1304
Current Amplification Factor, Variation with Emitter Current: Mar 616
Current Amplification versus Emitter Current and Junction Temperature: Nov 1875
Cutoff Frequency Measurement: Apr 780
Depletion Layer, Design Theory for: Jun 1422
Drift, Transient Response of: May 830
Effective Collector Capacitance in: Nov 1878
Five-Watt Ten-Megacycle: Jun 1209
FM Receiver, 150 MC: Apr 693
Internal Current Gain of Drift: Dec 1960
Junction Triode, Structure-Determined Gain Band Product of: Dec 1924
Lumped Models of: Jun 1141
Magnetic Core Binary Counter: Dec 1960
Measurement of Internal Temperature Rise of: Jun 1207
Micro-Alloy Diffused: Jun 1166

Monostable Multivibrators for Pulse Generation: Jun 1260
 Noise: Dec 1965
 Noise Figure Behavior: Feb 495
 Noise, Junction: Mar 589
 Noise in Junction: Jun 1019
 Oscillator Circuits, Junction, Design Basis for: Jun 1271
 Outdiffusion for Production of: Jun 1068
 Packaged in a Moist Atmosphere, Effect of Pulse Type Radiation on: Dec 1953
 Point-Contact, IRE Standards on Testing: May 878
 Power: Jun 1185
 Power, Effective Emitter Area of: Jun 1220
 Power, Saturation Voltages of: Jun 1304
 Properties of a Germanium Alloy-Diffused: Jun 1161
 Regulated Power Supplies: Aug 1537
 Research in Compound Semiconductors: Jun 959
 Research, Implications of: Jun 952
 Short-Circuit Current Gain and Phase Determination: Jun 1177
 Technological Impact of: Jun 955
 Tenth Anniversary of the: Jun 953
 Terminology and Notation, Need for Revision in: Dec 1949
 Thermal Resistance, Measurement of: Jun 1204
 Triodes, Germanium *N-P-I-N* Junction: Apr 783
 Two-Dimensional Current Flow at High Frequencies: Jun 1152
 Translation of Foreign Articles: May 917
 Transmission Error Function for Meteor-Burst Communication: Jul 1423
 Transmission Line, Shielded Balanced-Pair, Formulas for Capacitance of: May 922
 Transmission Lines, Suppression of Undesired Radiation of: Aug 1510
 Transmitters, AM, as SSB Jammers: Dec 1960
 Traps, Electrons, and Holes: Jun 973
 Traveling-Wave Tubes:
 Amplifier, Ferromagnetic: Apr 700
 Amplifier, Low-Noise Nonlinear Reactance: Sep 1655

Amplifier, Very Low-Noise: May 861
 Focusing Magnet, Leakage Flux Around: Oct 1751
 Frequency Range, Pumping to Extend: Jul 1420
 Periodically Focused, High Power: Feb 441
 S-Band, with Noise Figure Below 4 DB: May 911
 with Tapered Velocity Parameter: Sep 1658
 Trees in a Graph, Number of: Dec 1954
 Triggering Signals, Minimum: Sep 1654
 Triggering Signals, Minimum Energy: Apr 751
 Triode, *P-N* Junction, Advances in Understanding of: Jun 1130
 Triodes, Germanium *N-P-I-N* Junction Transistor: Apr 783
 Triodes, Silicon *P-N-P-N*, Electrical Characteristics of: Jun 1229
 Tropospheric Effects on 6-MC Pulses: Dec 1968
 Tropospheric Propagation at 400 MC, Long-Distance Overwater: Jul 1401
 Tropospheric Propagation, Report on URSI Commission II: Jul 1358
 TR Tubes, Improved Keep-Alive Design for: Jun 1309
 Tuning a Probe in a Slotted Line: Apr 787

U

Underground "Atmospherics": Nov 1870
 Undersea "Atmospherics": Nov 1870
 Utility in Government Research and Development: Jan 360

V

Varistors, Hyperbolic Analogs Using: Oct 1762
 Velocity Modulated Beam, Bunched Electron Current in: Aug 1536
 Velocity Modulation, Potential Well Theory of: Dec 1952
 Very-Low-Frequency Monopole Antenna, Earth Currents Near: Aug 1539
 Very-Low-Frequency Signals, Magneto-Ionic Duct Propagation Using: Apr 785
 Vessels, Filled, Statistics of: Nov 1873
 Vibrators, Piezoelectric, Measurement of the

Parameters of: Oct 1731
 Video Amplifiers with Stringent Electrical and Mechanical Requirements: Aug 1541
 Voltage Feedback in Junction Transistors: Jun 1305
 Voltage Sensitive Switch: Oct 1723

W

Wave Propagation:
 Airborne, Refraction Anomalies in: Sep 1628
 Astronomical Observations, Effects on: Jan 356
 Atmospheric Effects on VHF and UHF: Aug 1492
 Guided Submillimetric: Oct 1706
 Ionospheric, Report on URSI Commission III: Jul 1362
 Magneto-Ionic Duct, Using VLF Signals: Apr 785
 Short-Wave, Frequency Variations in: Dec 1934
 Transhorizon, Scattering Relationships in: Nov 1842
 Tropospheric Long-Distance Overwater at 400 MC: Jul 1401
 Tropospheric, Report on URSI Commission II: Jul 1358
 Unusual, at 40 MC from USSR Satellite: Mar 610
 VHF Off-Path: May 922
 Waveguides:
 Circular, Design of Conical Taper in: Mar 618
 Imperfect, Ghost Modes in: Feb 416
 Ion Filled, Properties of: Jan 360
 Parallel Plane, Partially Filled with a Dielectric: Dec 1953
 Taper Sections in Circular: Dec 1961
 Techniques Before 1900: Feb 405
 Waves, Elastic, in Thin Plates, Dispersion of High-Frequency: Dec 1965
 Westrex Stereophonic Disk System: Oct 1686
 Whistlers, Lightning Impulses which Produce: Oct 1760
 WWV Standard Frequency Transmissions: May 910, Jun 1309, Jul 1420, Aug 1534, Sep 1649, Oct 1758, Nov 1881, Dec 1950

NONTECHNICAL INDEX

Abstracts and References

Monthly Listings:
 January 386-400
 February 516-528
 March 676-688
 April 806-818
 May 933-946
 June 1332-1346
 July 1444-1458
 August 1556-1570
 September 1668-1682
 October 1780-1794
 November 1892-1906
 December 1980-1994

Abstracts of TRANSACTIONS

Monthly Listings:
 January 383-385
 February 512-515
 March 671-675
 April 798-805
 May 930-932
 June 1325-1331
 July 1438-1443
 August 1552-1555
 September 1665-1667
 October 1772-1779
 November 1888-1891
 December 1975-1979

Awards

Baker, W. R. G., Award:
 R. L. Kyhl: Jan 374, Apr 15A
 H. F. Webster: Jan 374, Apr 15A
 Diamond, Harry, Memorial Award:
 Edward W. Allen, Jr.: Apr 15A; Correction: Jun 15A
 Fellow Awards:
 Almqvist, M. L.: Apr 16A
 Auerbach, I. L.: Apr 16A

Beck, A. C.: Apr 16A
 Bereskin, A. B.: Apr 16A
 Breitwieser, C. J.: Apr 16A
 Brooks, F. E., Jr.: Apr 16A
 Brueckmann, H. L.: Apr 16A
 Clark, R. L.: Apr 16A
 Cole, R. I.: Apr 16A
 Costa, H.: Apr 18A
 Crain, C. M.: Apr 18A
 Davenport, W. B., Jr.: Apr 18A
 Dinger, H. E.: Apr 18A
 DiToro, M. J.: Apr 18A
 Epperson, J. B.: Apr 18A
 Fett, G. H.: Apr 18A
 Garman, R. L.: Apr 18A
 Gerber, E. A.: Apr 18A
 Gerks, I. H.: Apr 20A
 Giacchetto, L. J.: Apr 20A
 Giordano, A. B.: Apr 20A
 Haggerty, P. E.: Apr 20A
 Hall, A. C.: Apr 20A
 Herbstreit, J. W.: Apr 20A
 Hoepfner, C. H.: Apr 20A
 Honnell, P. M.: Apr 20A
 Horne, C. F.: Apr 20A
 Jasik, H.: Apr 22A
 Knoblauch, A. F.: Apr 22A
 Kohl, W. H.: Apr 22A
 Lyons, H.: Apr 22A
 Marcuvitz, N.: Apr 22A
 Marrison, W. A.: Apr 22A
 Miller, S. E.: Apr 22A
 Millman, J.: Apr 22A
 Mimno, H. R.: Apr 22A
 Moore, J. R.: Apr 24A
 Noble, H. V.: Apr 24A
 Pan, W. Y.: Apr 24A
 Peter, R. W.: Apr 24A
 Peterson, A. P. G.: Apr 24A
 Pipes, L. A.: Apr 24A
 Ramey, R. A., Jr.: Apr 24A
 Raymond, R. C.: Apr 24A

Reinartz, J. L.: Apr 24A
 Riblet, H. J.: Apr 26A
 Rochester, N.: Apr 26A
 Russell, J. B.: Apr 26A
 Scheldorf, M. W.: Apr 26A
 Schulz, E. H.: Apr 26A
 Seddon, J. C.: Apr 26A
 Selvidge, H.: Apr 26A
 Shank, R. J.: Apr 26A
 Sharpless, W. M.: Apr 26A
 Smale, J. A.: Apr 28A
 Soria, R. M.: Apr 28A
 Stoddart, R. R.: Apr 28A
 Sulzer, P. G.: Apr 28A
 Sunstein, D. E.: Apr 28A
 Tanner, R. H.: Apr 28A
 Toth, E.: Apr 28A
 Towner, O. W.: Apr 28A
 Tyson, B. F.: Apr 28A
 Van Deusen, G. L.: Apr 30A
 Waidelich, D. L.: Apr 30A
 Watkins, D. A.: Apr 30A
 Webb, R. C.: Apr 30A
 Weber, J.: Apr 30A
 Weihe, V. I.: Apr 30A
 Welch, H. W., Jr.: Apr 30A
 Wells, F. H.: Apr 30A
 Wilkins, A. F.: Apr 30A
 Winter, D. F.: Apr 32A
 Wright, J. W.: Apr 32A
 Zadeh, L. A.: Apr 32A
 Founders Award:
 W. R. G. Baker: Apr 14A
 Liebmman, Morris, Memorial Prize:
 Edward L. Ginzton: Apr 14A
 Medal of Honor:
 A. W. Hull: Apr 14A
 Thompson, Browder J., Memorial Prize:
 Arthur Karp: Apr 374, Apr 14A
 Zworykin, Vladimir K., Television Prize:
 Charles P. Ginsburg: Apr 15A; Correction: Jun 15A

Boards of Directors

1958 Officers and Directors Announced: Jan 374, Mar 658

Calendar of Coming Events

Monthly Listings:

January 374
February 505
March 658
April 34A
May 18A
June 14A
July 14A
August 14A
September 14A
October 14A
November 14A
December 14A

Committees

Membership Lists:

June 18A
October 30A

Representatives in Colleges:

June 30A
October 40A

Representatives on Other Bodies:

June 34A
October 44A

Technical Committee Notes:

Antennas and Waveguides: Jan 379
Audio Techniques: Jan 379
Circuits: Jan 379
Electron Tubes: Jan 379
Facsimile: Jan 379
Feedback Control Systems: Jan 379
Nuclear Techniques: Jan 379
Standards: Jan 379
Video Techniques: Jan 379

Conventions and Meetings

Acoustics Congress, Third International, Int'l Commission on Acoustics, Sep 1-8, 1959, Stuttgart, Germany: May 22A
Aeronautical and Navigational Electronics, Fifth Annual East Coast Conference, PGANE—Baltimore Section, Oct 27-28, 1958, Baltimore, Md.: Oct 26A
Aeronautical Communications Symposium, Fourth Annual, PGCS, Oct 20-22, Utica, N.Y.: Oct 20A
Aeronautical Electronics National Conference, May 12-14, 1958, Dayton, Ohio: May 24A
Analog Computer Conference, Int'l Assn. for Analog Computations, Sep 1-8, 1958, Strasbourg, France: Apr 34A
Automatic Control Techniques Joint Conference, AIEE—ASME—IRE, Apr 14-16, 1958, Detroit, Mich.: Mar. 658
Automatic Optimization Conference, ASME, Apr 2-4, 1958, Newark, Del.: Jan 375
Automation Exposition and Congress, Fourth International, Jun 9-13, 1958, New York City: Apr 36A
Broadcast Symposium, Eighth Annual, PGBTS, Sep 26-27, 1958, Washington, D.C.: Sep 26A
Circuit and Information Theory Symposium, PGCT—PGIT, Jun 16-18, 1959, Los Angeles, Calif.: Nov 16A
Cybernetics Congress, Second International, Sep 3-10, 1958, Namur, Belgium: May 22A
Eastern Joint Computer Conference, Dec 3-5, 1958, Philadelphia, Pa.: Nov 28A
Electrical Techniques in Medicine and Biology Conference, Eleventh Annual, PGME—AIEE—ISA, Nov 19-21, 1958, Minneapolis, Minn.: Sep 14A, Nov 28A
Electronic Components Conference, Apr 22-24, 1958, Los Angeles, Calif.: Mar 658
Electronic Standards and Measurements National Conference, PGI—Radio Standards Lab. of NBS—Electric and High-Frequency Instruments Committee of AIEE, Aug 13-15, 1958, Boulder, Colo.: Apr 38A, Jul 16A
Electronic Waveguides Symposium, Apr 8-10, 1958, New York City: Apr 40A
Engineering Writing and Speech Symposium, Second National, PGEWS, Oct 1-2, 1958, New York City: Sep 28A
Extended Range and Space Communications National Symposium, PGCS—PGAP—George Washington University, Oct 6-7, 1958, Washington, D.C.: Sep 28A

Global Communications Symposium, Second National, PGCS—Communications Division of AIEE, Dec 3-5, 1958, St. Petersburg Beach, Fla.: Nov 16A
Industrial Electronics Conference, Seventh Annual, IRE—AIEE, Sep 24-25, 1958, Detroit, Mich.: Sep 26A
Information Processing Conference, First International, UNESCO, Jun 15-20, 1959, Paris, France: Sep 16A
Institute of Radio Engineers Canadian Convention, Oct 8-10, 1959, Toronto, Canada: Jun 15A, Sep 22A
Institute of Radio Engineers Mid-America Electronics Convention, Kansas City Section, Nov 13-14, 1957, Kansas City, Mo.: Feb 506
Institute of Radio Engineers National Convention, Mar 24-27, 1958, New York City: Jan 375, Feb 505, Mar 622
Institute of Radio Engineers National Convention, Mar 23-26, 1959, New York City: Dec 14A
Magnetism and Magnetic Materials Conference, AIEE—APS—AIME—ONR—PGMTT, Nov 17-20, 1958, Philadelphia, Pa.: Nov 20A
Medical Electronics International Conference, Jun, 1958, Paris, France: Nov 15A
Microwave Theory and Techniques National Symposium, PGMTH, May 5-7, 1958, Stanford, Calif.: Jan 378, Apr 42A
Military Electronics Convention, Second National, PGMIL, Jun 16-18, 1958, Washington, D.C.: Feb 507, May 32A, Sep 16A
National Electronics Conference, Fourteenth Annual, IRE—AIEE—Ill. Inst. of Tech.—Illinois University—Northwestern University, Oct 13-15, 1958, Chicago, Ill.: Sep 16A, Oct 14A
National Simulation Conference, PGEC—Dallas Section, Oct 23-25, 1958, Dallas, Tex.: Jun 18A, Oct 24A
Nonlinear Magnetics and Magnetic Amplifiers Special Technical Conference, AIEE, Aug 6-8, 1958, Los Angeles, Calif.: May 22A
Northeast Electronics Research and Engineering Meeting, Boston, Conn., and Western Mass. Sections, Nov 19-20, 1958, Boston, Mass.: Nov 24A
Nuclear Science Meeting, Fifth Annual, PGNS, Nov 6-7, 1958, San Mateo, Calif.: Oct 28A
Polytechnic Institute of Brooklyn, Microwave Research Institute, Eighth Annual International Symposium, Apr 8-10, 1958, New York City: Jan 376
Polytechnic Institute of Brooklyn, Microwave Research Institute, Ninth Annual International Symposium, Mar 31, Apr 1-2, 1959, New York City: Dec 14A
Production Techniques Conference, Second National, PGPT, Jun 4-6, 1958, New York City: May 30A
Radio Aids to Aeronautical and Marine Navigation Convention, Institution of Electrical Engineers, Mar 27-28, 1958, Longon, England: Jan 376
Radio Fall Meeting, Oct 27-29, 1958, Rochester, N.Y.: Oct 24A
Radio Noise Spectrum Conference, Harvard College Observatory, Apr 22, 1958, Cambridge, Mass.: Apr 36A
Region 3 Technical Meeting, Nov 17-18, 1958, Atlanta, Ga.: Nov 18A
Reliable Electrical Connections Conference, EIA, Dec 2-4, 1958, Dallas, Tex.: Oct 14A
Scintillation Counter Symposium, IRE—AIEE—ABC—NBS, Jan 27-28, 1958, Washington, D.C.: Jan 378
Semiconductor Symposium, Seventh Annual, Electrochemical Society, May 3-7, 1959, Philadelphia, Pa.: Nov 16A
Silicon Carbide Conference, AFCRC, Apr 2-3, 1959, Boston, Mass.: Oct 16A
Southwestern IRE Conference and Electronics Show, Tenth Annual, Apr 10-12, 1958, San Antonio, Tex.: Jan 375, Mar 661, Apr 40A, Jul 14A
Telemetering National Symposium, PGTRC, Sep 22-24, 1958, Miami Beach, Fla.: Aug 16A
Television and Transistors Technical Conference, Twelfth Annual, PGBTS—PGBTR—Cincinnati Section, Apr 18-19, 1958, Cincinnati, Ohio: Mar 658, Apr 36A
Transistor and Solid State Circuits Conference, Feb 20-21, 1958, Philadelphia, Pa.: Feb 508
Transistors and Associated Semiconductor Devices International Convention, Radio

and Telecommunication Section of IEE, May 25-29, 1959, London, England, Nov 14A

URSI Fall Meeting, URSI—PGIT—PGAP, Oct 21-22, 1958, University Park, Pa.: Sep 14A, Oct 20A
USA-URSI Spring Meeting, Apr 24-26, 1958, Washington, D.C.: Mar 659
Vehicular Communications Annual Conference, PGVC, Dec 4-5, 1958, Chicago, Ill.: Nov 26A
Weather Radar Conference, American Meteorological Society—Marine Lab. of the University of Miami, Nov 17-20, 1958, Miami Beach, Fla.: Jul 15A
Western Electronics Show and Convention, IRE—West Coast Electronic Manufacturers' Assn., Aug 19-22, 1958, Los Angeles, Calif.: Jun 16A, Jul 18A, Aug 15A
Western Joint Computer Conference, IRE—AIEE—Assn. for Computing Machinery, May 6-9, 1958, Los Angeles, Calif.: Mar 659, Aug 16A, Oct 16A

Front Covers

Beyond-Horizon Measurements at Sea: July
Giant Long-Range Horn Antenna: August
IRE Symbols: March
JTAC 10th Anniversary: May
Junction Transistor: June
Light Patterns Reflected from a Recorded Disc: December
Motional Modes of Piezoelectric Crystals: April
Photomicrograph of Stereophonic Disk Grooves: October
Picture Produced by Experimental Solid-State Display Panel: November
Pre-1900 Microwave Antenna: February
Radio Telescope and Spiral Nebula: January
Thermoelectron Engine: September

Frontispieces

Baker, W. R. G.: Mar 532
Brown, Gordon S.: Jul 1348
Cole, Ralph I.: Nov 1796
Doherty, William H.: Jun 948
Fink, Donald G.: Jan 2
Fowler, Glenn A.: Aug 1460
Grandqvist, Carl E.: Feb 404
Hull, Albert W.: Mar 533
Newton, Kenneth V.: May 820
Oxley, Allan B.: Oct 1684
Ryder, John D.: Apr 690
Schulz, Elmer H.: Dec 1908
Sinclair, Donald B.: Sep 1572

IRE People

Adams, G. J.: Sep 46A
Adams, R.: Dec 50A
Aiken, W. S.: Dec 54A
Alexander, B.: Nov 68A
Anderson, F. J.: Jun 54A
Anderson, J. R.: Aug 26A
Astin, A. V.: Oct 80A
Attwood, S. S.: Dec 36A
Backus, A. S.: Oct 62A
Bailey, G. W.: Feb 14A
Baker, W. R. G.: Feb 20A, Oct 62A
Baldwin, E. M.: May 56A
Barnard, G. A., III: Nov 84A
Barney, K. H.: Feb 30A
Bauer, B. B.: Jun 46A
Begovich, N. A.: Jul 82A
Behnke, A. O.: Sep 46A
Belcher, H. P.: Nov 64A
Bennett, B. J.: Nov 84A
Bertan, L. L.: Nov 58A
Bibbero, R. J.: Jul 78A
Bode, H. W.: Dec 40A
Boss, L. J.: May 58A
Bowie, R. M.: Jun 56A
Bowman, J. Y.: Oct 68A
Boyd, J. A.: Nov 104A
Breitwieser, C. J.: Nov 102A
Brockner, C. E.: Feb 30A
Brooks, F. A., Jr.: Sep 50A
Brown, A. S.: Sep 42A
Brown, F. W.: Oct 80A
Brugman, W. E.: Nov 50A
Burtness, R. W.: Jun 52A
Busignies, H.: Aug 26A, Sep 46A, 58A
Calvert, J. F.: Nov 48A
Casabona, A. M.: Nov 68A
Caswell, J. N.: Feb 30A
Chapin, M. F.: Mar 38A

Christiansen, C. L.: Oct 62A
 Clark, M. E.: Jun 44A
 Clavier, A. G.: Sep 46A, 58A
 Coe, W. G.: Dec 58A
 Combellick, T. A.: Jun 48A
 Cookson, A. E.: Nov 68A
 Cottony, H. V.: Oct 80A
 Coven, A. W.: Feb 16A
 Cushman, E. A.: Jun 54A
 Davis, E. L.: Dec 36A
 Dean, N. J.: Jun 44A
 Dennis, P. A.: Nov 56A
 De Rosa, L. A.: Sep 58A
 De Vore, C.: Apr 56A
 Dillon, J. D.: Aug 26A
 Doherty, W. H.: Jul 74A
 Dow, W. G.: Dec 36A
 Duerig, W. H.: Jul 84A
 Dyke, E.: May 46A
 Dyke, W. P.: Oct 72A, Nov 52A
 Ebert, J. E.: May 60A
 Edgerly, J. J.: Aug 26A
 Edwards, C. M.: Mar 42A
 Eisler, G.: Nov 101A
 Ellefson, B. S.: Mar 52A
 Engelmann, H. F.: Nov 50A
 Everingham, L. R.: Aug 48A
 Fellendorf, G. W.: Jul 68A
 Fink, E. A.: Nov 62A
 Friedland, M. S.: Jan 24A
 Friedman, S. L.: Apr 52A
 Friis, H. T.: Apr 52A
 Furth, F. R.: Apr 50A
 Gaw, N. W., Jr.: Jun 48A
 Gifford, R. P.: Mar 50A
 Giordano, A. F.: Jul 76A
 Glover, A. M.: Jul 71A
 Goldsmith, A. N.: Dec 52A
 Goldstone, L. O.: Feb 16A
 Goode, H. H.: Nov 72A
 Gough, L. E.: Nov 68A
 Gould, R. V.: Feb 30A
 Grabbe, E. M.: Nov 56A
 Guterman, F. H.: Jan 20A
 Hagen, J. P.: Aug 28A
 Haller, G. L.: May 50A
 Harris, H., Jr.: May 53A
 Hartman, F. B.: Oct 54A
 Hartong, H.: Jan 26A
 Harvey, N. L.: Nov 80A
 Heiden, C. M.: Mar 15A
 Hendershot, L. R.: Nov 64A
 Henderson, J. A.: Nov 68A
 Henkels, H. W.: Aug 28A
 Hennies, S. R.: Feb 14A
 Hertzberg, J. M.: Apr 50A
 Hewlett, W. R.: Mar 12A
 Hicks, B. A.: Dec 54A
 Hiestand, N. P.: Aug 34A
 Hilliard, J. K.: Mar 12A
 Hillier, J.: Apr 50A
 Himmel, L.: Nov 68A
 Hobbs, M.: Oct 54A
 Hockeimer, H. E.: May 48A
 Hogan, C. L.: May 64A
 Hull, D. R.: Apr 50A
 Humeniuk, P.: May 53A
 Huntoon, R. D.: Dec 34A
 Ide, J. M.: Jul 68A
 Jenkins, J. F., Jr.: May 46A
 Jensen, A. G.: Nov 100A
 Joe, R. H.: Oct 80A
 Johnson, H. R.: Mar 12A, 15A
 Johnson, R. R.: Nov 84A
 Johnson, R. W.: May 46A
 Johnson, S. O.: Jun 44A
 Jordan, J. P.: Nov 80A
 Kamen, L.: Dec 30A
 Kandoian, A. G.: Sep 58A
 Kapust, L. A.: Mar 54A
 Kearney, J. W.: Apr 50A
 Kebby, M. H.: Oct 78A
 Kelly, M. J.: Sep 42A
 Kiebert, M. V.: Feb 14A
 Kinzie, Mrs. M. E.: Mar 23A
 Knowles, C. H.: May 62A
 Kock, W. E.: Mar 42A
 Kovach, L. D.: Aug 34A
 Lack, F. R.: Nov 101A, Dec 48A
 Landis, V., Jr.: Jan 24A, Oct 74A
 Lanier, H. F.: Jun 68A
 Larson, C. C.: Nov 68A
 Lasher, C. C.: Sep 54A
 Lehr, P. N.: Mar 18A
 Leifer, M.: Dec 46A
 Leiper, J. H.: Jul 66A
 Lester, J. M.: Feb 30A
 Levine, A. M.: Sep 58A
 Liston, K. L.: Nov 68A

Lowe, M. E.: Jun 64A
 Lutz, C. H.: Jan 20A
 Machol, R. E.: Nov 62A
 MacKechnie, H. K.: Aug 34A
 Malter, L.: Jul 76A, Sep 54A
 Marshall, R. A.: Oct 80A
 Masnaghetti, R. K.: Dec 30A
 Masurat, G.: Nov 50A
 Mayfield, J. D.: Aug 40A
 McFall, R. W.: Mar 26A
 McKay, K. G.: Dec 58A
 McMullen, C. G.: Mar 44A
 McPherson, W. R.: Aug 26A
 McRae, J. W.: Nov 88A
 McWhorter, A. L.: Dec 56A
 Meisinger, H. P.: Jun 46A
 Melville, R. W.: Nov 84A
 Mercer, W. R.: Jul 66A
 Metcalf, G. F.: Oct 78A
 Milner, C. M.: Jun 48A
 Miggins, C. R.: Mar 26A
 Mitchell, H. F., Jr.: Oct 74A
 Molnar, J. P.: Nov 88A
 Morris, F. W., Jr.: Apr 58A, Aug 42A
 Morton, J. A.: Dec 40A
 Mueller, G. J.: Oct 76A
 Nellis, S.: Dec 50A
 Norton, J. M.: Jan 28A
 Nottingham, W. B.: Aug 46A
 Ogilvie, A. R.: Jun 56A
 Oldfield, H. R., Jr.: Sep 54A
 Omberg, A. C.: Mar 42A
 Orman, L. M.: Jul 71A
 Packard, D.: Sep 50A
 Paganelli, T. L.: Jun 60A
 Parry, R. Y.: Apr 58A
 Patterson, G. K.: Oct 54A
 Pearson, R. W.: Oct 58A
 Pecorini, R. R.: Aug 48A
 Perkins, G. O.: Dec 30A
 Petrusek, A. C.: May 62A
 Phillips, T. L.: Jul 66A
 Pietenpol, W. J.: Oct 70A
 Piller, S. E.: Oct 54A
 Platts, G. F.: Mar 34A
 Powers, J. S.: Jan 12A
 Preist, D. H.: Nov 86A
 Ragazzini, J. R.: Jul 66A
 Ramo, S.: Feb 14A
 Reade, R. B.: Nov 62A
 Reber, J. H.: Aug 48A
 Reedy, P. H.: Feb 16A
 Rempt, H.: Nov 68A
 Renton, R. J.: May 46A
 Rhoads, J. A.: Oct 76A
 Rice, H.: Jun 64A
 Richardson, H. L.: Mar 52A
 Richmond, M. R.: Jul 66A
 Risse, J. A.: Jan 12A
 Robel, M. C.: Jun 72A
 Robinson, W. H.: Sep 50A
 Rochester, N.: Nov 48A
 Rosselot, G. A.: Mar 42A
 Rosser, T. N.: Jun 52A
 Russell, L.: Sep 46A
 Sackman, R.: Sep 60A, Oct 66A
 Saliba, J. R.: May 58A
 Sanders, R. C., Jr.: Jul 66A
 Sandretto, P. C.: Sep 58A
 Scheil, R. H.: Mar 30A
 Schenck, H. H.: Mar 48A
 Schlesinger, A. K.: Sep 54A
 Schooley, A. H.: May 60A
 Schultz, J. L.: Nov 76A
 Schwennesen, D. O.: Sep 50A
 Seldin, L.: Jun 72A
 Serniuk, W.: Oct 54A
 Shannon, C. E.: Dec 52A
 Sichak, W.: Nov 68A
 Sinclair, G.: Jul 68A
 Skrivseth, A. G.: May 46A
 Slaughter, G. K.: Feb 30A
 Smith, B., Jr.: Feb 28A
 Smith, J. S.: Feb 30A
 Snyder, R. L.: Feb 28A
 Speakman, E. A.: Mar 38A
 Spencer, P. L.: Mar 18A
 Spool, J.: Aug 42A
 Spriggs, A. J.: Dec 50A
 Steen, J. R.: Oct 68A
 Stout, H. L.: Mar 30A
 Strickland, H. A., Jr.: Sep 54A
 Strum, P. D.: Dec 56A
 Teachman, A. E.: Jun 68A
 Terman, F. E.: Mar 12A
 Thompson, A. J.: May 48A
 Torn, L. J.: Mar 48A
 Toth, E.: Feb 20A
 Towlson, H. G.: Jan 12A

Trapp, J. A.: Nov 58A
 Troxel, R.: Jan 20A
 Uhrhane, F. F.: Dec 56A
 Urey, G.: Jan 26A
 Velesky, J. J.: Nov 56A
 Von Tersch, L.: Jun 44A
 Warnecke, R. R.: Aug 46A
 Watkins, D. A.: Mar 12A
 Waynick, A. H.: Dec 30A
 Weber, E.: Mar 34A, Sep 48A
 Welkowitz, W.: Nov 68A
 Welter, N. E.: Mar 30A
 Whitehorn, R. M.: Nov 86A
 Whitelock, L. D.: Nov 56A
 Wilmotte, R. M.: Jul 73A
 Winter, N. L.: May 64A
 Woodbury, W. F.: May 56A
 Wrye, W. F., Jr.: Jan 26A
 Young, H. A.: Jun 70A
 Ziegler, G. E.: Sep 48A

Miscellaneous

Bailey, G. W., Awarded Honorary Degree by Lawrence College: Aug 14A
 Black, H. S., Wins Lamme Gold Medal: Jul 15A
 Catholic University Appoints Research Coordinator: Nov 16A
 Cooper, B. F. C., Awarded the 1957 Norman W. V. Hayes Memorial Medal: Mar 659
 Cosentino, Adolfo T., New Argentine Minister of Communications: Nov 14A
 Engstrom, E. W., Wins Medal: Jan 375
 Eta Kappa Nu Pays Tribute to Two Young IRE Members: Jan 376
 Graf, Alois W., Death Mourned by IRE Board of Directors, a Resolution: Feb 505
 Henry, Eugene Walter, Awarded Renewal of PCEC Fellowship: Jun 18A
 IRE Fellows Automatically Entitled to AAAS Fellowship: Jun 15A
 IRE Ten-Year Club: Apr 34A
 Israel Section Cosponsors Third National Convention of Electronic Engineers: Dec 16A
 Kaar, I. J., Is Recipient of IRE-EIA Fall Meeting Plaque: Feb 505
 McDowell, L. S., Is the First Woman to Become Life Member: Feb 506
 NEC Awards Second Fellowship: Jul 14A
 NEC Elects Top 1958 Officers: Jun 16A
 Roberts, F. B., Receives Award from Professional Group on Broadcast and Television Receivers: Jan 378
 Seventh Region IRE Conference and Trade Show Emphasized Electronics Progress: May 22A
 Society for the History of Technology Is Formed: Jul 15A
 Tolles, W., Wins Recognition for Work on Cytoanalyzer: Jan 376
 Wayne University Joins NEC: May 18A
 WESCON Officers Are Chosen: Mar 660
 WESCON Names Committeemen: Apr 38A
 Young, L. C., and Horton, J. W., Receive Highest Navy Civilian Award: Jun 16A

Notices

Air Force MARS Eastern Technical Net Announces Programs: Jan 374, Feb 507, Mar 659, Apr 34A, Sep 16A, Oct 16A, Nov 15A, Dec 18A
 Army MARS Technical Net Announces Programs: Sep 15A, Oct 16A, Nov 14A, Dec 18A
 Bibliographical Bulletin on Computers Available: Jan 374
 Computers in Control Systems Conference Proceedings Are Available: Aug 14A
 Electron Devices Meeting, 1958, Solicits Papers: Apr 38A
 Electronics Components and Materials Conference Solicits Papers and Abstracts: Sep 15A
 Engineering Writing and Speech Symposium Calls for Papers: Jun 18A
 Institute of Mathematical Sciences Offers Temporary Memberships for Research: Feb 506
 IRE Canadian Convention to Publish Technical Papers: Nov 18A
 IRE Miscellaneous Publications Available: May 18A, Oct 15A
 IRE National Convention Papers Deadline Announced: Jul 14A, Aug 14A, Sep 14A, Oct 14A
 IRE National CONVENTION RECORD for 1958 to Appear: Apr 46A
 IRE Standards Available: Dec 15A

Library of Congress Changes Names of Two Publications: May 22A
 Magnetism and Magnetic Materials Conference Calls for Papers: Jun 18A
 Michigan University Gives Course in Automatic Control: Apr 34A
 M.I.T. Offers Summer Program on Switching Circuits: Apr 36A
 National Simulation Conference Calls for Papers: Mar 659
 Nuclear Congress of 1959 Asks for Abstracts by October 1: Aug 16A
 Nuclear Science Meeting Calls for Papers: Jun 18A, Jul 15A
 PGMIL Convention Proceedings Available: Oct 14A
Research Management, New Journal, Appears: Aug 16A
 Solid-State Circuits Conference Sets Deadline for Abstracts: Sep 15A
 Southwestern IRE Conference Proceedings Available: May 18A
 Soviet Periodicals Available in English Translations: Jan 376, Jun 15A, Oct 16A
 Strato-Lab Symposium Invites Papers: Dec 16A
 WESCON Convention Record to Be Published: Sep 20A
 WESCON Papers Deadline Set: Mar 658, Apr 34A

Obituaries

Barkley, William J.: Apr 38A
 Burnside, Don G.: Aug 16A
 Campbell, Charles A.: Mar 661
 Exon, Frank Cecil: Sep 20A
 Freeman, E. E.: Feb 507
 Gilbert, John J.: Feb 507
 Gustafson, Gilbert E.: Jul 15A
 Hallborg, Henry E.: Oct 18A
 Jensen, John C.: Jan 379
 Lawrence, Ernest O.: Nov 18A
 LeVelle, Alfred S.: Apr 38A
 Link, Louis J.: Aug 16A
 Lippincott, Donald K.: Dec 18A
 Metzger, Frederick W.: Mar 661
 Pegram, George Braxton: Oct 18A
 Webb, Wilbur L.: Mar 661

Photographs

Aeronautical Communications Symposium Executive Committee: Oct 16A
 Aeronautical Communications Third Symposium Participants: Feb 507
 Bailey, G. W., Receives Honorary Degree: Aug 14A
 Baltimore Mayor Presents Airborne Electronics Week Proclamation Honoring Fifth Annual East Coast Conference on Aeronautical and Navigational Electronics: Nov 16A
 Bramhall, F. B., and J. E. Boughtwood, Winners of the 1957 D'Humy Medal: Jan 377
 Buenos Aires Section's Officers and Adolfo T. Cosentino: Nov 14A
 Collings, F.: May 30A
 Cytoanalyzer and Douglas Sprunt: Jan 376
 Dingley, E. N., Jr., IRE Chairman of GLOBE-COM II: Nov 16A
 Engelman, Capt. Chris (Ret.), Introduces Dr. S. W. Horwald at PGMIL Luncheon: Sep 18A
 Firth, Adm. Fritz (U.S.N. Ret.) and Rear Adm. W. E. Cleaves (Ret.) at PGMIL Convention: Sep 18A
 Florida West Coast Section's Newly-Elected Officers: Sep 15A
 Garcia, I. L., AIEE Chairman of GLOBE-COM II: Nov 16A
 Haller, G. L., and T. C. Rives, at Banquet of the National Aeronautical and Navigational Electronics Conference: Sep 16A
 Holaday, William M., Addresses PGMIL Banquet: Sep 18A
 Horton, J. W.: Jun 16A
 IRE Board of Directors: Sep 18A
 IRE National Convention and Radio Engineering Show of 1958 in Pictures: May 14A-16A
 Jensen, Neils, Models Space Chamber Suit for WESCON Program: Aug 15A
 Kaar, I. J.: Feb 505
 MAECON Exhibit and Observers: Feb 506
 McDowell, L. S.: Feb 506
 Microwave Theory and Techniques 1958 National Symposium Steering Committee: Apr 44A

Military Electronics Second National Convention Executive Committee: May 32A
 NEREM Committee Members: Nov 15A
 Neuschaefer, G. C.: Jan 377
 North Carolina Section's New Officers: Jan 377
 Northern New Jersey Section Toured by President Fink: May 22A
 Novak, W. D.: May 30A
 Ollendorff, H., Delivers Paper at Israel's Third National Convention of Electronic Engineers: Dec 16A
 PGBTS Cleveland Chapter Meets at WERE Radio Station: Jan 377
 PGBTS Fall Symposium Participants: Jan 377
 Reliability and Quality Control Symposium Discussed by Program Chairman, Keynote Speaker, and General Chairman: May 20A
 Rome-Utica Section's Officers Entertain D. G. Fink: Oct 15A
 Rynda, Ted: Feb 507
 San Francisco Chapter of the PGMIL Holds Discussion: Jun 14A
 San Francisco Section's Officers: Sep 20A
 Scott Helt Award Presented at Broadcast Symposium: Dec 14A
 Southwestern IRE Conference Committee: Mar 661
 Swiggett, R. L.: May 30A
 Transistor Conference at Philadelphia: Jun 14A
 Transistor-Solid State Circuits Conference Program Committee: Mar 660
 Trinkaus, J. W.: May 30A
 Tucker, Durward, and John McNeely, Conference Chairman and Exhibits Chairman of 1959 Southwestern IRE Conference and Electronics Show: Sep 18A
 U. S. Program Committee for 1959 International Conference on Information Processing: Sep 16A
 Vannah, W. E.: May 30A
 Washington Section Award Presentation at Annual Banquet: May 20A
 WESCON Attended by D. G. Fink and Chairmen of Los Angeles and San Francisco Sections: Dec 15A
 WESCON Executive Committee for 1958: Mar 660
 WESCON Officials: May 20A
 Young, L. C.: Jun 16A

Poles and Zeros

Editor, The
Abstracts and References, Listings of Technical Papers: Jan 1
 Advertising and IRE Publications: Oct 1683
 Backwards Space: Mar 531
 Board of Directors May Meeting: Aug 1459
 Board of Directors September Meeting: Nov 1795
 Down-Under Land: May 819
 Editorial Survey: May 819
 Elections for IRE Regional Directors: Nov 1795
 Engineering Shortage, 1962?: Dec 1907
 Engineering Surplus?: Jun 947
 Engineers' Council for Professional Development and Its Program: Oct 1683
 Format Changes: Apr 689
 Future of Engineering Education: Sep 1571
 Growth of IRE and Electronics Field: Jul 1349
 High School Students: Mar 531
 History of Batteries: Sep 1571
 IRE Convention: Mar 531
 IRE International Scope: Mar 531
 IRE Standards: Feb 403
 Membership Application Blank in New Directory: Dec 1907
 Radio Astronomy Special Issue: Jan 1
 Ramsay, John F., Paper Entitled "Microwave Antenna and Wave Guide Techniques Before 1900": Feb 403
 Scanning the TRANSACTIONS: Mar 531
 Section Number Ninety-Nine Approved: Sep 1571
 Section Number One Hundred Approved: Nov 1795
 Shows and Symposia: Dec 1907
 Standards and IRE Standards: Nov 1795
 Student Awards: Apr 689
 Students and High Schools: Feb 403
 TRANSACTIONS and Progress of Electronics: Aug 1459
 Transistors Special Issue: Jun 947
 Travel Is Broadening: Apr 689

Travelogue Continue: May 819
 WESCON: Aug 1459

Professional Groups

Chairmen:
 January 380
 March 666
 May 36A
 July 24A
 September 30
 November 30A
 News:
 Aeronautical and Navigational Electronics: Mar 661
 Broadcast Transmission Systems: Jul 15A
 Circuit Theory: Mar 661, May 22A, Jun 18A
 Communications Systems: Jan 375, Mar 661, Apr 38A, Jul 15A
 Electronic Computers: Apr 38A
 Engineering Writing and Speech: Feb 507, Mar 661, Jun 18A, Jul 15A
 Industrial Electronics: Mar 661
 Human Factors in Electronics: Mar 661
 Medical Electronics: Jun 18A, Aug 16A
 Microwave Theory and Techniques: Mar 661
 Military Electronics: Jun 18A, Jul 15A, Nov 18A
 Radio Frequency Interference: Jan 378, Nov 18A
 Telemetry and Remote Control: Apr 38A
 Ultrasonic Engineering: Aug 16A
 Vehicular Communications: Apr 38A, Nov 18A

Report of Secretary

Letter to Board of Directors, 1957: Jun 1318

Scanning the Issue

Monthly Notes:
 February 402
 March 530
 April 691
 May 821
 June 949
 July 1349
 August 1461
 September 1573
 October 1685
 November 1797
 December 1909

Scanning the TRANSACTIONS

Monthly Notes:
 February 510
 March 669
 April 792
 May 926
 June 1317
 July 1434
 August 1545
 September 1661
 October 1768
 November 1885
 December 1972

Sections and Subsections

Chairmen and Secretaries:
 January 381
 March 666
 May 36A
 July 26A
 September 30A
 November 32A
 News (See also *Photographs*):
 Anchorage Section Approved: Nov 15A
 Berkshire Subsection Becomes Full Section: Jan 375
 Colombian Section Approved: Mar 658
 Connecticut Valley Section Changes Name to Connecticut Section: Jan 375
 Erie and Western Michigan Sections Formed: Mar 658
 Fairfield County Subsection of Connecticut Section Established: Nov 15A
 Hampton Roads Subsection Replaced by Burlington Subsection: Jan 375
 Merrimack Valley Subsection of Boston Section Approved: Nov 15A
 Quebec Subsection Becomes 100th Section: Nov 15A
 Santa Ana Subsection of Los Angeles Section Formed: Mar 658
 South Carolina Section Formed: Jul 14A

INDEX TO BOOK REVIEWS

Listings are by month and page.

- Acoustical Engineering, by H. F. Olson (*Reviewed by B. B. Bauer*): Jan 380
- Acoustics, by J. L. Hunter (Title only): Mar 565
- Analysis and Control of Nonlinear Systems, by Y. A. Ku (*Reviewed by T. M. Stouf*): Jul 1436
- Analytical Design of Linear Feedback Controls, by G. C. Newton, Jr., L. A. Gould, and J. F. Kaiser (*Reviewed by A. M. Hopkin*): Feb 508
- Applied Analysis, by C. Lanczos (Title only): Mar 665
- Applied Statistics for Engineers, by W. Volk (Title only): May 929
- Atmospheric Explorations, edited by H. G. Houghton (*Reviewed by A. W. Straiton*): Aug 1547
- Automatic Digital Computers, by M. V. Wilkes (Title only): May 929
- Automatic Process Control, by D. P. Eckman (Title only): Dec. 1975
- Automation and Management, by J. R. Bright (*Reviewed by J. J. Lamb*): Jun 1324
- L'Automatique des Informations, by F. H. Raymond (*Reviewed by J. P. Jeanneney*): Jun 1324
- Basic Automatic Control Theory, by G. J. Murphy (Title only): Aug 1552
- Basic Electric Circuit Theory, by W. W. Lewis with the assistance of C. F. Goodheart (*Reviewed by A. B. Giordano*): May 928
- Basic Electrical Engineering, by R. H. Nau (*Reviewed by A. V. Eastman*): Jul 1437
- Basic Electricity for Communications, by W. H. Timbie, 2nd ed., revised by F. J. Ricker (Title only): Aug 1552
- Basic Pulses, by I. Gottlieb (Title only): Dec 1975
- Basic Television, Vols. I-V, by A. Schure (Title only): May 929
- Basics of Digital Computers, Vols. 1-3, by J. S. Murphy (Title only): Oct 1772
- Le Calcul Analogique par Courants Continus, by D. Dumesnils (*Reviewed by B. Lippel*): Oct 1771
- Calculus for Electronics, by A. E. Richmond (Title only): Aug 1552
- Ceramic Fabrication Processes, edited by W. D. Kingery (Title only): Apr 797
- Circuit Analysis of Transmission Lines, by J. L. Stewart (*Reviewed by H. A. Wheeler*): Oct 1769
- Closed Circuit TV System Planning, by M. A. Mayers and R. D. Chipp (*Reviewed by F. J. Bingley*): May 928
- Comprehensive Bibliography on Operations Research, A, by Operations Research Group, Case Institute of Technology (Title only): Oct 1772
- Computability and Unsolvability, by M. Davis (Title only): Oct 1772
- Conference on Extremely High Temperatures, edited by Heinz, Fischer, and Mansur (Title only): Oct 1772
- Control Engineering Manual, edited by B. K. Ledgerwood and Staff of Control Engineering (Title only): Apr 797
- Control Engineer's Handbook, edited by J. G. Truxal (*Reviewed by J. M. Salzer*): Aug 1551
- Digital Computer Components and Circuits, by R. K. Richards (*Reviewed by W. B. Cagle*): Apr 796
- Digital Differential Analyzers, by G. F. Forbes, 4th ed. (Title only): Mar 665
- Direction of Research Establishments, The. Proceedings of a symposium held in 1956 in England (Title only): Aug 1552
- Distributed Amplification, by H. Stockman, 2nd ed. (Title only): Mar 665
- Dry-Battery Receivers with Miniature Valves, by E. Rodenhuis (Title only): Mar 665
- Economics of Atomic Energy, by M. S. Goldberg (Title only): Mar 665
- Einführung in die Mikrowellen-Elektronik, Teil II: Lauffeldröhren, by W. Kleen and K. Pöschl (*Reviewed by W. J. Albersheim*): Sep 1663
- Electric Conduction in Semiconductors and Metals, by W. Ehrenberg (Title only): Oct 1772
- Electrical Discharges in Gases, by F. M. Penning (*Reviewed by J. D. Cobine*): May 929
- Electron Tube Materials Compilation of ASTM Standards (Title only): Dec 1975
- Electron Tubes and Semiconductors, by J. J. DeFrance (Title only): May 929
- Electronic Components Handbook, edited by K. Henney and C. Walsh (*Reviewed by R. R. Batcher*): Mar 663
- Electronic Designers' Handbook, by R. W. Landee, D. C. Davis, and A. P. Albrecht (Title only): Aug 1552
- Electronic Measuring Instruments, by E. H. W. Banner (Title only): Oct 1772
- Electronic Semiconductors, by E. Spenke, translated by D. Jenny, H. Kroemer, E. G. Ramberg, and A. H. Sommer (*Reviewed by G. C. Dacey*): Aug 1550
- Electronics in Industry, by G. M. Chute, 2nd ed. (Title only): Mar 665
- Electrostatics, edited by A. Schure (Title only): Oct 1772
- Elektronenröhren, by M. J. O. Strutt (*Reviewed by W. H. von Aulock*): Apr 796
- Elements of Magnetic Tape Recording, by N. M. Haynes (*Reviewed by F. A. Comerct*): Jun 1323
- Elements of Tape Recorder Circuits, by H. Burstein and H. C. Pollak (Title only): Apr 797
- Elsevier's Dictionary of Electronics and Waveguides, compiled by W. E. Clason (Title only): Apr 797
- Encyclopedia of Radio and Television, The (*Reviewed by P. Mertz*): Jul 1438
- Engineering College Research Review—1956, edited by R. Contini (*Reviewed by H. H. Goode*): Jun 1322
- Engineering Electronics, by J. D. Ryder (*Reviewed by J. J. Gershon*): Mar 664
- English-Russian, Russian-English Electronics Dictionary, compiled by Department of the Army (*Reviewed by P. E. Green, Jr.*): Dec 1974
- Exploration of Space by Radio, The, by R. H. Brown and A. C. B. Lovell (*Reviewed by F. T. Haddock*): Aug 1546
- Faisceaux Hertzien et Systèmes de Modulation, by L. J. Libois (*Reviewed by J. B. Lair*): Nov 1886
- Feedback Control Systems, by O. J. M. Smith (*Reviewed by G. S. Axelby*): Aug 1549
- Feedback Theory and Its Applications, by P. H. Hammond (*Reviewed by J. E. Bertram*): Dec 1973
- Finite Queuing Tables, by L. G. Peck and R. N. Hazelwood (Title only): Aug 1552
- F.M. Radio Servicing Handbook, by G. J. King (Title only): Oct 1772
- Fundamental Principles of Transistors, by J. Evans (*Reviewed by F. H. Blecher*): Jul 1435
- Fundamentals of Electron Devices, by K. R. Spangenberg (*Reviewed by L. J. Giacletto*): Mar 664
- Fundamentals of Transistors, by L. Krugman, 2nd ed. (Title only): Dec 1975
- Gas Tubes, edited by A. Schure (Title only): Dec. 1975
- Glass Engineering Handbook, by E. B. Shand (Title only): Dec 1975
- Handbook of Calculus, Difference and Differential Equations, by E. J. Cogan (Title only): May 929
- Handbook of Noise Control, edited by C. M. Harris (*Reviewed by V. Wouk*): May 927
- Handbook of Piezoelectric Crystals for Radio Equipment Designers, by J. P. Buchanan (Title only): May 929
- High Fidelity: A Bibliography of Sound Reproduction, by K. J. Spencer (Title only): Oct 1772
- High Fidelity Simplified, by H. D. Weiler, 3rd ed. (Title only): Mar 665
- High Quality Sound Reproduction, by J. Moir (Title only): Dec 1975
- Ideas, Inventions and Patents, by R. A. Buckles (Title only): Mar 665
- Impedance Matching, by A. Schure (Title only): Aug 1552
- Impulse und Schaltvorgänge in der Nachrichtentechnik, by H. Kaden (*Reviewed by G. C. Sziklai*): Mar 663
- Industrial Control Circuits, by S. Platt (Title only): Aug 1552
- Industrial Electronics Circuits, by R. Kretzmann (*Reviewed by W. L. Atwood*): May 927
- Industrial Electronics Handbook, 2nd ed. (*Reviewed by W. L. Atwood*): May 927
- Industrial Television, by H. A. McGhee (Title only): Oct 1772
- Information Theory Third London Symposium—1955, edited by C. Cherry (Title only): Apr 797
- Installing Electronic Data Processing Systems, by R. G. Canning (Title only): Mar 665
- Introduction to Automatic Computers, An, by N. Chapin (Title only): Mar 665
- Introduction to Combinatorial Analysis, An, by J. Riordan (Title only): Aug 1552
- Introduction to Digital Computers, An, by R. K. Livesley (*Reviewed by W. B. Cagle*): Aug 1548
- Introduction to Electromagnetic Engineering, by R. F. Harrington (*Reviewed by L. A. Manning*): Sep 1662
- Introduction to Electromagnetic Fields, by S. Seely (*Reviewed by A. B. Haines*): Oct 1771
- Introduction to Functional Analysis, by A. E. Taylor (Title only): Dec 1975
- Introduction to Heat Transfer, by A. I. Brown and S. M. Marco, 3rd ed. (Title only): Apr 797
- Introduction to Nonlinear Analysis, by W. J. Cunningham (Title only): Oct 1772
- Introduction to Operations Research, by C. W. Churchman, R. L. Ackoff, and E. L. Arnoff (Title only): May 929
- Introduction to Probability Theory and Its Applications, An, Vol. I, by W. Feller, 2nd ed. (*Reviewed by R. M. Fano*): Mar 662
- Introduction to Semiconductors, An, by W. C. Dunlap, Jr. (*Reviewed by S. N. Van Voorhis*): May 927
- Introduction to the Theory of Random Signals and Noise, An, by W. B. Davenport, Jr. and W. L. Root (*Reviewed by W. M. Siebert*): Aug 1547
- Introduction to Transistor Circuits, by E. H. Cooke-Yarborough (*Reviewed by H. E. Tompkins*): Mar 662
- Introductory Electrical Engineering, by G. F. Corcoran and H. R. Reed (Title only): Apr 797
- Ionization and Breakdown in Gases, by F. Llewellyn-Jones (Title only): Mar 665
- Ionosphere, The, by K. Rawer (*Reviewed by W. Pfister*): Apr 795
- ju* or Symbolic Method, The, by H. Stockman (Title only): Mar 665
- Logical Design of Digital Computers, by M. Pfister, Jr. (*Reviewed by R. A. Tracy*): Jun 1323
- Magnetic-Amplifier Circuits, by W. A. Geyger (Title only): May 929
- Magnetic Tape Recording, by H. G. M. Spratt (*Reviewed by A. Meyerhoff and K. McIlwain*): Dec 1974
- Management Approach to Electronic Digital Computers, The, by J. S. Smith (*Reviewed by J. J. Lamb*): Jun 1324
- Manual of Scientific Russian, by T. F. Magner (Title only): Oct 1772
- Marine Radar, by D. G. Lang (Title only): Apr 797
- Mass Spectroscopy, by H. E. Duckworth (*Reviewed by H. C. Maltrow*): Sep 1662
- Mathematics and Computers, by G. R. Stibitz and J. A. Larrivee (*Reviewed by J. R. Weiner*): Mar 664
- Mathematics for Radio and Electronics, by F. M. Colebrook and J. W. Head (Title only): Mar 665
- Measurement of Colour, The, by W. D. Wright (*Reviewed by W. T. Winttingham*): Jun 1325
- Microwave Measurements, by E. L. Ginztan (*Reviewed by A. B. Giordano*): Feb 508
- Microwave Transmission Design Data, by T. Moreno (Title only): Oct 1772
- Missile Engineering Handbook, by C. W. Beserer (*Reviewed by C. H. Hoepfner*): Nov 1887
- Modern Computing Methods (*Reviewed by L. N. Ridenour*): Sep 1663

- Nomograms of Complex Hyperbolic Functions, by J. Rybner, 2nd ed. (Reviewed by M. Katsin): Feb 509
- Nonlinear Control Systems, by R. L. Cosgriff (Reviewed by T. M. Slout): Oct 1770
- Notes on Analog-Digital Conversion Techniques, edited by A. K. Susskind (Reviewed by C. T. Leondes): Apr 796
- Nuclear Engineering, edited by C. F. Bonilla (Title only): Mar 665
- Nuclear Rocket Propulsion, by R. W. Bussard and R. D. DeLauer (Title only): Dec 1975
- 1956 National Symposium on Vacuum Technology Transactions, edited by E. S. Perry and J. H. Durant (Title only): Apr 797
- Operational Mathematics, by R. V. Churchill, 2nd ed. (Title only): Oct 1772
- Ordinary Difference-Differential Equations, by E. Pinney (Title only): Apr 797
- Oscilloscope Techniques, by A. Haas (Title only): Oct 1772
- Passive Network Synthesis, by J. E. Storer (Reviewed by P. F. Ordung): May 929
- Photosensors, by W. Summer (Reviewed by F. Koury): Aug 1550
- Physics and Mathematics in Electrical Communication, by J. O. Perrine (Title only): Aug 1552
- Physique Electronique des Gaz et des Solides, by M. Bayet (Reviewed by J. I. Pankove): Aug 1546
- Perception and Communication, by D. E. Broadbent (Title only): Oct 1772
- Piezoelectricity, by the General Post Office Research Station (Reviewed by H. Jaffe): Oct 1770
- Principles of Electrical Measurements, by H. Buckingham and E. M. Price (Reviewed by G. B. Hoadley): Aug 1547
- Principles of Electricity, by L. Page and N. I. Adams, Jr., 3rd ed. (Reviewed by E. T. Jaynes): Sep 1664
- Principles of Electronic Instruments, by G. R. Partridge (Reviewed by W. Richter): Aug 1549
- Principles of Noise, by J. J. Freeman (Reviewed by W. D. White): Oct 1771
- Printed Circuitry, by A. Lytel (Title only): May 929
- Proceedings of the EIA Conference on Maintainability of Electronic Equipment (Title only): Aug 1552
- Proceedings of the EIA Symposium on Numerical Control Systems for Machine Tools (Title only): May 929
- Proceedings of the Fourth Annual Computer Applications Symposium (Title only): Aug 1552
- Proceedings of the 1957 National Electronics Conference, Vol. 13 (Title only): Aug 1552
- Proceedings of the Twelfth General Assembly, Vol. XI, Part 1, Commission I on Radio Measurements and Standards (Title only): Aug 1552
- Proceedings of the Twelfth General Assembly, Vol. XI, Part 5, Commission V on Radio-astronomy (Title only): Oct 1772
- Programming for an Automatic Digital Calculator, by K. H. V. Booth (Reviewed by D. Combello): Nov 1886
- Progress in Semiconductors, Vol. I, edited by A. F. Gibson, P. Aigrain, and R. E. Burgess (Title only): Apr 797
- Progress in Semiconductors, Vol. II, edited by A. F. Gibson, P. Aigrain, and R. E. Burgess (Reviewed by L. T. DeVore): Apr 794
- Propagation Troposphérique, by G. Boudouris (Reviewed by G. Deschamps): Jul 1435
- Pulse and Digital Circuits, by J. Millman and H. Taub (Title only): Apr 797
- Radio Aids to Air Navigation, by J. H. H. Grover (Reviewed by H. Busignies): Jun 1323
- Radio Amateur's Handbook, The, 35th ed. (Title only): May 929
- Radioisotopes, A New Tool for Industry, by S. Jefferson (Title only): May 929
- Receiving Aerial Systems, by I. A. Davidson (Reviewed by C. E. Smith): Mar 662
- Science of Engineering Materials, The, edited by J. E. Goldman (Reviewed by L. T. DeVore): Jan 379
- Scientific and Technical Translating and Other Aspects of the Language Problem, by UNESCO (Reviewed by W. N. Locke): Apr 797
- Scientific Programming in Business and Industry, by A. Vazsonyi (Title only): Oct 1772
- Selection and Application of Metallic Rectifiers, by S. P. Jackson (Reviewed by J. T. Cataldo): Mar 663
- Semiconductors—Their Theory and Practice, by G. Goudet and C. Meuleau, translated from the French by G. King (Previously reviewed in its original edition by D. A. Jenny in PROC., Jul 1957; Title only): Mar 665
- Serial Publications of the Soviet Union 1939–1957, A Bibliographic Checklist, compiled by R. Smits (Title only): Oct 1772
- Solid State for Engineers, The, by M. J. Sinnott (Reviewed by J. S. Saby): Oct 1769
- Solid State Physical Electronics, by A. van der Ziel (Reviewed by A. R. Moore): May 929
- Solid State Physics, by A. J. Dekker (Reviewed by F. Herman): Jan 379
- Solid State Physics, Vol. II, edited by F. Seitz and D. Turnbull (Title only): Mar 665
- Solid State Physics, Vol. IV, edited by F. Seitz and D. Turnbull (Reviewed by L. T. DeVore): Feb 509
- Sourcebook on Atomic Energy, by S. Glasstone, 2nd ed. (Title only): May 929
- Soviet Education for Science and Technology, by A. G. Korol (Reviewed by E. Weber): Aug 1548
- Space Charge Waves and Slow Electromagnetic Waves, by A. H. W. Beck (Reviewed by J. R. Pierce): Dec 1973
- Stereophonic Sound, by N. H. Crowhurst (Reviewed by B. B. Bauer): Apr 794
- Structure and Policy of Electronic Communications, The, by D. W. Smythe (Title only): Mar 665
- Switching Circuits and Logical Design, by S. H. Caldwell (Reviewed by R. W. Stuart): Nov 1887
- Synthesis of Passive Networks, by E. A. Guillemin (Reviewed by S. Darlington): Jul 1435
- Technical Report Writing, by J. W. Souther (Reviewed by J. D. Chapline): Jul 1438
- Television Engineering, Vol. IV: General Circuit Techniques, by S. W. Amos and D. C. Birkinshaw (Reviewed by E. T. Jaynes): Dec 1974
- Television in Science and Industry, by V. K. Zworykin, E. G. Ramberg, and E. L. Flory (Reviewed by R. D. Chipp): Oct 1770
- Theorie der Spulen und Übertrager, by R. Feldtkeller (Title only): Dec 1975
- Theory of Dielectrics, by H. Frohlich, 2nd ed. (Title only): Aug 1552
- Theory of Networks in Electrical Communication and Other Fields, The, by F. E. Rogers (Reviewed by E. A. Guillemin): Jul 1437
- Transients in Electrical Circuits, by G. V. Lago and D. L. Waidelich (Reviewed by G. B. Herzog): Sep 1663
- Transistor A. F. Amplifiers, by D. D. Jones and R. A. Hilbourne (Title only): Aug 1552
- Transistor Circuits and Applications, by J. M. Carroll (Reviewed by R. P. Burr): Mar 662
- Transistor Electronics, by D. DeWitt and A. L. Rossoff (Reviewed by A. P. Stern): Jun 1322
- Transistor Physics and Circuits, by R. L. Riddle and M. P. Ristenbatt (Reviewed by A. Warnick): Jul 1437
- Ultra High Frequency Performance of Receiving Tubes, The, by W. E. Benham and I. A. Harris (Reviewed by R. D. Wilson): Jul 1436
- Vacuum Tube Rectifiers, by A. Schure (Title only): Aug 1552
- Van Nostrand's Scientific Encyclopedia, 3rd ed. (Reviewed by G. Shapiro): Aug 1551
- Zone Melting, by W. G. Pfann (Reviewed by D. A. Jenny): Aug 1549

Index to

IRE NATIONAL CONVENTION RECORD

Volume VI, 1958



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TABLE OF CONTENTS

Part 1	
Antennas and Propagation, Microwaves.....	3
Part 2	
Circuit Theory, Ultrasonics.....	3
Part 3	
Electron Devices.....	3
Part 4	
Automatic Control, Computers, Information Theory.....	3
Part 5	
Aeronautical, Instrumentation, Telemetry.....	4
Part 6	
Components, Industrial Electronics, Production, Reliability.....	4
Part 7	
Audio, Broadcast, Receivers.....	5
Part 8	
Communications, Military, Radio Frequency Interference.....	5
Part 9	
Medical Electronics, Nuclear Science.....	5
Part 10	
Education, Writing and Speech, Management.....	5
Index to Authors.....	6
Index to Subjects.....	7
1958 IRE NATIONAL CONVENTION RECORD Prices.....	12

IRE NATIONAL CONVENTION RECORD

CONTENTS OF VOLUME VI—1958

Part 1—Antennas and Propagation, Microwaves

Atomic Clocks and Masers	
A Gas Cell Atomic Clock Using Optical Pumping and Optical Detection, <i>M. Arditi and T. R. Carver</i>	3
The Atomichron®—An Atomic Frequency Standard: Physical Foundations, <i>A. O. McCoubrey</i>	10
The Atomichron®—An Atomic Frequency Standard: Operation and Performance, <i>W. Mainberger and A. Orenberg</i>	14
Analysis of the Emissive Phase of a Pulsed Maser, <i>H. H. Theissing, F. A. Dieler, and P. J. Caplan</i>	19
A Two-Cavity Unilateral Maser Amplifier, <i>N. Sher</i>	27
Microwave Measurements	
Power Limiting Using Ferrites, <i>R. F. Soohoo</i>	36
An Ultraprecise Microwave Interferometer, <i>G. R. Blair</i>	48
Direct Reading Microwave Phase-Meter, <i>H. A. Dropkin</i>	57
A Microwave Spin Resonance Spectrometer, <i>R. R. Unterberger</i>	64
The Use of Impulse Response in Electromagnetic Scattering Problems, <i>E. M. Kennough and R. I. Cosgriff</i>	72
Microwave Components	
A New Microwave Rotary Joint, <i>W. E. Fromm, E. G. Fubini, and H. S. Keen</i>	78
High Power, Broadband, Microwave Gas Discharge Switch Tube (Summary), <i>S. J. Tetenbaum and R. M. Hill</i>	83
High Power Microwave Filters, <i>J. H. Vogelman</i>	84
A Band Separation Filter for the 225–400 MC Band, <i>A. I. Grayzel</i>	91
Direct-Coupled, Band-Pass Filters with $\lambda/4$ Resonators, <i>G. L. Malthaei</i>	98
Propagation and Antennas I	
Extreme Useful Range of VHF Transmission by Scattering from the Lower Ionosphere, <i>R. C. Kirby</i>	112
Meteor Burst Propagation, <i>J. T. deBettencourt, A. E. Ward, and B. Goldberg</i>	121
The Duty Cycle Associated with Forward-Scattered Echoes from Meteor Trails, <i>H. J. Wirth and T. J. Keary</i>	127
Cap-Loaded Folded Antenna, <i>E. W. Seely, J. D. Burns, and K. L. Welton</i>	133
Logarithmically Periodic Antenna Designs, <i>R. H. DuHamel and F. R. Ore</i>	139
Phase Center of Helical Beam Antennas, <i>S. Sander and D. K. Cheng</i>	152
Antennas II	
Early Warning Radar Antennas, <i>J. M. Flaherty and E. Kadak</i>	158
Phase and Amplitude Measurements in the Near Field of Microwave Lenses, <i>C. W. Morrow, P. E. Taylor, and H. T. Ward</i>	166
Annular Slot Direction-Finding Antenna, <i>H. H. Hougardy and N. Yaru</i>	177
A Novel Antenna for Mobile Radio Relay Operation in the UHF Range, <i>F. J. Triolo</i>	183
Lightweight High-Gain Antenna, <i>R. G. Malech</i>	193
Voltage Breakdown Characteristics of Microwave Antennas (Abstract), <i>J. B. Chown, T. Morita, and W. E. Scharfman</i>	199
Antennas III—Microwave Antennas	
A Compact Dual-Purpose Antenna, <i>W. A. Meyer, W. G. Scott, and W. O. Puro</i>	200
A Volumetric Electrically Scanned Two-Dimensional Microwave Antenna Array, <i>J. L. Spradley</i>	204
Closely Spaced High Dielectric Constant Polyrod Arrays, <i>L. W. Mickey and G. G. Chadwick</i>	213
Waveguide Loaded Surface Wave Antenna, <i>R. F. Hyneman and R. W. Hougardy</i>	225
Image Line Surface Wave Antenna, <i>H. W. Cooper, M. Hoffman, and S. Isaacson</i>	230
A Dual Beam Planar Antenna for Janus Type Doppler Navigation Systems, <i>H. Saltzman and G. Stavits</i>	240

Part 2—Circuit Theory, Ultrasonics

Circuit Theory II—Unusual Aspects of Filter Design	
Multichannel-Filter Synthesis in Terms of Dipole Potential Analog, <i>H. A. Wheeler</i>	3
Minimum Insertion Loss Filters, <i>E. G. Fubini and E. A. Guillemín</i>	11
A New Approach to the Design of High Frequency Crystal Filters, <i>R. A. Sykes</i>	18
Synthesis of Active RC Single-Tuned Bandpass Filters, <i>J. J. Bongiorno</i>	30
A New Class of Filters, <i>A. Papoulis</i>	42
Circuit Theory III—Application of Topological and Group Concepts	
Signal Flow Graph and Network Topology—How to Avoid Them, <i>O. Wing</i>	48
New Transpositions in Power Transformer Windings, <i>R. G. deBuda</i>	54
Two-Terminal Pair Symmetry Relations, <i>R. C. Kiessling</i>	61
Analysis of Nonreciprocal Networks by Digital Computer, <i>W. Mayeda and M. E. Van Valkenburg</i>	70
On Non-Series-Parallel Realization of Driving-Point Function, <i>W. H. Kim</i>	76
Circuit Theory I and Ultrasonics I—Symposium on Modern Aspects of Delay Lines	
Low-Dispersion Wired Delay Lines, <i>M. J. DiToro</i>	82

Electrical Design of the Transducer Networks of a Magnetostrictive Delay Line, <i>L. Rosenberg and A. Rothbart</i>	92
The Approximation Problem in Lumped Delay Lines, <i>A. Papoulis</i>	102
Coiled Wire Torsional Wave Delay Line, <i>R. N. Thurston and L. M. Tornillo</i>	109
Variable Delay Line Using Ultrasonic Surface Waves, <i>J. D. Ross, S. J. Kapuscinski, and K. B. Daniels</i>	118
Ultrasonics II—Delay Line Measurements	
Measurements in Delay in Ultrasonic Systems, <i>D. L. Arenberg</i>	121
Precise Measurement of Time Delay, <i>J. E. May</i>	134
The Measurement of Delay-Line Transducer Resistance, <i>J. J. G. McCue and J. A. Leavitt</i>	143
Ultrasonic-Delay-Line Terminating Circuits and Passband Measurements, <i>M. Axelbank</i>	147
Temperature and Frequency Dependence of Insertion Loss in Delay Lines, <i>A. H. Meitzler</i>	153
The Measurement of the Total Spurious Responses of an Ultrasonic Delay Line, <i>M. S. Zimmerman</i>	161
Ultrasonics III—Measurement of Radiated Acoustic Power	
The Power Handling Capability of Ferroelectric Ceramics, <i>G. W. Renner, R. A. Plante, and T. F. Hueter</i>	167
Measurement of Acoustic Power Radiated from Underwater Sound Transducers, <i>R. J. Bobber</i>	185
An Instrument for Measuring Intensity of Ultrasound, <i>J. F. Her-rick, B. H. Anderson, and M. Neher</i>	189
Measurements of Acoustic Power in Industrial Ultrasonic Equipment, <i>W. Welkowitz</i>	199
Problems in Power Measurement (Abstract), <i>G. E. Henry, S. E. Jacke, F. Massa, and M. Strasberg</i>	210

Part 3—Electron Devices

Beam and Display Tubes	
High Transconductance Wideband Television Gun, <i>E. Atti</i>	3
The Annular Geometry Electron Gun, <i>J. W. Schwartz</i>	13
Recent Developments in Shaped Beam Display and Recording Techniques, <i>R. M. Peterson and R. C. Ritchart</i>	21
ELF—A New Electroluminescent Display, <i>E. A. Sack</i>	31
The Tube That Tells Time, <i>W. Eriksen and E. Handly</i>	40
Semiconductor Devices	
A New Passive Semiconductor Component, <i>R. M. Warner, Jr.</i>	43
Use of the RCA 2N384 Drift Transistor As a Linear Amplifier, <i>D. M. Griswold and V. J. Cadra</i>	49
High Current Switching Times for a P-N-P Drift Transistor: Numerical Analysis on the IBM 704 Digital Computer, <i>A. Mitchell and L. Lapidus</i>	57
A New High Frequency Diffused Base N-P-N Silicon Transistor, <i>J. J. Sardella and R. C. Womson</i>	68
A New Five-Watt, Class A, Silicon Power Transistor, <i>P. Flaherty, G. Freedman, P. Kaufmann, D. Root, D. Spillehouse, W. Waring, P. Whoriskey, and J. Williams</i>	77
Microwave Tubes	
Noise Characteristics of a Backward-Wave Oscillator, <i>J. B. Cicchetti and J. Munushian</i>	84
The Pulsed M-Type Backward-Wave Oscillator and Its Modes of Operation, <i>G. Klein and A. L. Winters</i>	94
The Estiatron—An Electrostatically Focused Medium-Power Traveling-Wave Tube, <i>D. Blattner and F. Vaccaro</i>	101
The Generation of Shaped Pulses Using Microwave Klystrons, <i>D. H. Preist</i>	106
Wide Band UHF 10 KW Klystron Amplifier, <i>H. Goldman, L. F. Gray, and L. Pollack</i>	114

Part 4—Automatic Control, Computers, Information Theory

Tutorial Session on Detection Theory and Its Applications	
Detection As a Statistical Decision Problem (Abstract), <i>D. Van Meter</i>	3
Some Communications Applications of Detection Theory (Summary), <i>W. B. Davenport, Jr.</i>	4
Some Applications of Detection Theory to Radar, <i>W. M. Siebert</i>	11
Human Factors in Detection and in Speech Communication in Noise, <i>J. P. Egan</i>	115
Information Theory: Coding and Detection	
On Communication Processes Involving Learning and Random Duration, <i>R. Bellman and R. Kalaba</i>	116
The Application of "Comparison of Experiments" to Detection Problems, <i>N. Abramson</i>	22
Signals with Uniform Ambiguity Functions, <i>R. M. Lerner</i>	27
Evaluation of Some Error Correction Methods Applicable to Digital Data Transmission, <i>A. B. Brown and S. T. Meyers</i>	37
Algebraic Decoding for a Binary Erasure Channel, <i>M. A. Epstein</i>	56
Statistical Applications	
Frequency-Domain Statistical Model of Linear Variable Networks for Finite Operating Time, <i>G. W. Johnson</i>	70
The Root Square Locus Plot—A Geometrical Method for Synthesizing Optimum Servo Systems, <i>S. S. L. Chang</i>	79
TV Bandwidth Reduction by Digital Coding, <i>W. F. Schreiber and C. F. Knapp</i>	88

Subjective Experiments in Visual Communication, <i>R. E. Graham</i>	100
Demonstration of Some Visual Effects of Using Frame Storage in Television Transmission (Abstract), <i>M. W. Baldwin, Jr.</i>	107
Educational Needs in Systems Engineering	
Panel Discussion, <i>R. P. Johnson, H. Chestnut, H. H. Goode, S. Herwald, R. J. Kochenburger, W. K. Linvill, and J. Moore</i>	108
Automatic Control—General	
A Servo-Pressure Control System for the Iron Lung, <i>G. A. Biernson and J. E. Ward</i>	126
Gain-Phase Relations of Nonlinear Circuits, <i>E. Levinson</i>	141
On the Design of Adaptive Systems, <i>H. L. Groginsky</i>	160
Systems Considerations for Computers in Process Control, <i>E. L. Braun and G. Post</i>	168
A Self-adjusting System for Optimum Dynamic Performance, <i>G. W. Anderson, J. A. Aseltine, A. R. Mancini, and C. W. Sarture</i>	182
Computers and Control	
A Preventive Maintenance Program for Large General Purpose Electronic Analog Computers, <i>R. P. Sykes</i>	191
The TRICE—A High Speed Incremental Computer, <i>J. M. Mitchell and S. Ruhman</i>	206
Digital Moon-Radar Antenna Programmer with Analog Rate Signal Integrator, <i>O. Gutzmann</i>	217
A Balanced Precision Reference Regulator for Computer Application, <i>D. A. Noden</i>	225
A Solid-State Analog-to-Digital Conversion Device, <i>M. Palevsky</i>	232
Imaginary Axis Translation of Transfer Functions, <i>J. L. Ryerson</i>	236
Magnetics and Computers	
A High Speed N-Pole, N-Position Magnetic Core Matrix Switch, <i>A. L. Lane and A. Turcsyn</i>	246
Apertured Plate Memory: Operation and Analysis (Abstract), <i>W. J. Haneman, J. Lehmann, and C. S. Warren</i>	254
Molecular Storage and Read-out with Microwaves, <i>C. H. Becker, R. L. Pierce, and J. R. Martin</i>	255
Calculation of Flux Patterns in Ferrite Multipath Structures, <i>S. A. Abbas and D. L. Critchlow</i>	263
Logic by Ordered Flux Changes in Multipath Ferrite Cores, <i>N. F. Lockhart</i>	268
Flux Responsive Magnetic Heads for Low Speed Read-out of Data, <i>L. W. Ferber</i>	279
General Systems	
Combat Computers, <i>W. F. Luebbert</i>	292
The USAF Automatic Language Translator, Mark I, <i>G. Shiner</i>	296
Nonbinary Switching Theory, <i>O. Lowenschuss</i>	305
Automatic Type Size Normalization in High Speed Character Sensing Equipment, <i>A. I. Terso</i>	318
Minimum Time Programming on a Drum Computer, <i>B. Shiffman</i>	327

Part 5—Aeronautical, Instrumentation, Telemetry

Telemetry and Remote Control	
The RCA Flight Data System, <i>C. N. Batsel, Jr., R. E. Montijo, Jr., and E. J. Smuckler</i>	3
A Pulse Position Telemetry System, <i>L. Weisman and E. Teltscher</i>	11
Sample-and-Hold Circuits for Time Correlation of Analog-Voltage Information, <i>W. T. Eddins</i>	21
A Transistorized Six-Channel Airborne Digitizer, <i>S. H. McMillan and W. A. Sutton</i>	26
Channel Selection for Multi-Carrier Telemetry, <i>L. S. Taylor and G. F. Bigelow</i>	34
Telemetering Receiving Station Time Pulse Detector, <i>J. Star</i>	43
Aeronautical and Navigational Electronics I	
A Vortac Air Traffic Control System, <i>P. E. Ricketts</i>	50
Airborne Vortac Distance Measuring Equipment for the Federal Airways System, <i>S. H. Dodginton and B. B. Mahler</i>	55
Integrated Defense, Early Warning, Air Traffic Control System, <i>B. H. Baldridge and E. V. Hogan</i>	63
The AN/APN-96 Doppler Radar Set, <i>M. W. McKay</i>	71
Increasing the Traffic Capacity of Transponder Systems, <i>H. Davis and M. Setvin</i>	80
Aeronautical and Navigational Electronics II	
Airborne Dual Antenna System for Aerial Navigation (Summary), <i>W. M. Spanos and J. M. Ashbrook</i>	94
Engineering Evaluation of an Automatic Ground Controlled Approach System (AN/MNS-3), <i>R. M. Brooks and W. F. Hoy</i>	95
A Quantitative Analysis of Automatic Target Detection-Position Estimation Schemes Observing Scintillating Targets in Noise, <i>C. M. Waller</i>	107
Applying the Amplitron and Stabiutron to MTI Radar Systems, <i>T. A. Weil</i>	120
Transistorized Airborne Frequency Standard, <i>G. R. Hykes</i>	131
Instrumentation Systems	
An Earth Satellite Instrumentation for Cloud Measurements, <i>R. A. Hanel and R. A. Stampff</i>	136
A Precise Optical and Radar Tracking Range, <i>E. V. Kullmann</i>	142
A High-Speed Radar-Signal Measurement and Recording System, <i>A. Nirenberg, S. Perlman, and R. Burfeind</i>	150
A High Performance Multichannel Instrumentation System, <i>W. G. Wolber</i>	158
Instrumentation Dynamically Analyzed for Optimum Reliability, Weight and Geometric Space Envelope Subjected to Severe Vibrations and Shock, <i>D. Ehrenpreis</i>	167
Data Reduction and Recording	
Instrumentation for Recording and Analysis of Audio and Subaudio Noise, <i>D. D. Howard</i>	176
A Xerographic Cathode-Ray-Tube Recorder, <i>H. H. Hunter, O. A. Ullrich, and L. E. Walkup</i>	183
Theory of Magnetography, <i>S. J. Begun</i>	190
Application of Magnetography to Graphic Recording, <i>J. B. Gehman</i>	198

A Shaft Position Digitizer System of High Precision, <i>L. G. deBey and R. C. Webb</i>	204
A High Precision Digital Shaft Position Indicator, <i>D. H. Raudenbush</i>	211
High-Accuracy Instruments, Measurement and Calibration	
A Feedback Amplifier with Negative Output Resistance for Magnetic Measurements, <i>W. P. Harris and I. L. Cooler</i>	217
Millimicrosecond, Wide-Aperture, Electro-optical Shutter, <i>J. A. Hull</i>	228
A Quartz Servo Oscillator, <i>N. Lea</i>	234
A New Method to Simplify Bridge Type Measurements on Quartz Crystal Units, <i>E. Hafner</i>	243
RF Voltmeter Calibrating Consoles, <i>M. C. Selby, L. F. Behrent, and F. X. Ries</i>	251
Electronics in Space	
Propulsion and Interplanetary Travel (Title Only), <i>S. Chapman and H. Preston-Thomas</i>	258
Man in the Space Environment (Title Only), <i>D. G. Simons</i>	258
Communications and Telemetering (Title Only), <i>J. B. Wiesner</i>	258
Terminal Environment (Title Only), <i>F. L. Whipple</i>	258
The IGV and Space Technology (Title Only), <i>L. V. Berkner</i>	258
Electronics in Space Technology, <i>C. S. Draper</i>	259

Part 6—Components, Industrial Electronics, Production, Reliability

Advances in Production Engineering	
Automatic Transistor Classifier, <i>F. J. Morcerf and L. F. Roehm</i>	3
Packaging and Integration of Transistor Assemblies, <i>H. H. Hagens</i>	12
Automatic Soldering Machine for Printed Circuit Board Assemblies, <i>W. L. Oates</i>	20
Some Economic Aspects of Wire Processing for Low Volume Production of Electronic Gear, <i>J. Bension and R. D. Peters</i>	26
Case History, <i>T. C. Combs</i>	34
Tension in Coil and Tape Winding, <i>E. J. Saxl</i>	39
Reliability Through Components	
Reliability of Missile Guidance Systems—The Statistical Cliché vs Reality, <i>A. R. Gray</i>	49
Component Part Failure Rate Analysis for Prediction of Equipment Mean Life, <i>R. L. Vander Hamm</i>	72
A Progress Report on the Arma Inertial Guidance System Reliability Program, <i>E. F. Derfinger</i>	77
An Impulse Test for Evaluating the Vibrational Characteristics of Receiving Tubes over a Wide Frequency Range, <i>S. A. Jolly and W. U. Shipley</i>	90
Reliability of Power Amplifier Klystrons in Tropo-scatter Communication Systems, <i>R. F. Lazzarini and H. A. Bailey</i>	108
Reliability Through Systems	
On an Analytical Design Technique, <i>J. B. Heyne</i>	118
Reliability and Longevity for Space Technology, <i>A. R. Matthews</i>	123
Reliability Improvement Through Redundancy at Various System Levels, <i>B. J. Flehinger</i>	137
Fundamental Techniques in Doppler Radar Navigation System Reliability Measurements, <i>P. D. Stahl</i>	152
Reliability Prediction and Test Results on USAF Ground Electronic Equipment, <i>J. J. Naresky</i>	165
Electronic Component Parts	
Development of Electronic Components for the Nuclear Radiation Environment, <i>J. W. Clark</i>	178
Design of Shielded Air-Cored Inductors (Summary), <i>R. O. Schildkraut</i>	186
Ceramic Coating Applications in the Electrical Field, <i>P. A. Hupperl</i>	187
The Components Engineer and the Sales Engineer, Partners in Reliability, <i>P. C. Knox</i>	196
Miniature Ruggedized Precision Meters, <i>J. F. Faughnan and R. E. Laiselle</i>	198
Electronic Component Parts	
Effect of High Intensity Radiation on Electronic Parts and Materials (Summary), <i>C. P. Lascaro and A. L. Long</i>	206
Some Guideposts to the Use of Metallized Capacitors, <i>W. C. Lamphier</i>	207
New Amplifiers for Automatic Control of Active DC Loads, <i>E. Levi</i>	216
Magnetostriction Transducers for Mechanical Filters, <i>R. L. Sharma and H. O. Lewis</i>	223
Application of Piezoelectric Resonators to Modern Band-Pass Amplifiers, <i>A. Lungo and K. W. Henderson</i>	235
The Canadian Automation System of Postal Operations	
The Canadian Automation System of Postal Operations (Abstract), <i>M. Levy</i>	243
Coding and Error Checking in the Canadian System (Abstract), <i>M. Levy and V. Czorny</i>	244
Organization of the Electronic Computer for the Canadian Automated Mail Handling System, <i>A. Barszczewski</i>	245
"Facing" Machine Circuits; an Electrostatic Printer for Code-Marking Letters, and Fluorescent Ink and Optical Considerations in a Code Reader, <i>H. Jensen, K. H. Ulyall, and D. F. Steadman</i>	259
Industrial Electronics	
Chairman's Introduction, <i>E. W. Leaver</i>	273
Distributor Test Stand, <i>J. A. Lovell</i>	274
A Digital Setting System for an X-Ray Thickness Gauge, <i>V. A. Blumhagen</i>	280
Application of Magnetic Core Logic to Industrial Controls, <i>H. Tellefsen and S. Alessio</i>	283
A Coordinated System of Automatic Control Accessories, <i>R. R. Baucher</i>	294
Electronics Systems in Industry—A Panel Discussion	

Industrial Electronics and Education, <i>J. D. Ryder</i>	302
Electronic Systems and the American Economy, <i>C. C. Hurd</i>	307
Industrial Electronics Systems, <i>T. R. Jones</i>	310
Can Industrial Electronics Help to Conserve Technical Manpower? <i>J. M. Bridges</i>	314

Part 7—Audio, Broadcast, Receivers

Broadcast Transmission Systems	
Video Modulation Limiter (Abstract), <i>L. S. Sadler</i>	3
Color TV Recording on Magnetic Tape (Abstract), <i>J. L. Greuer</i>	4
An Automatic Level Control Using Vertical Interval Test Signals, <i>J. R. Popkin-Churman and F. Davido</i>	5
Remote Control of a Broadcast Transmitter and Directional Antenna System, <i>I. L. Ross</i>	12
Use of a Sectionalized TV Tower in AM Broadcast Service, <i>A. C. Goodnow</i>	14
Broadcast Transmission Systems and Communication Systems	
Remote Controlled 50-KW Broadcast Transmitter, <i>R. N. Harmon</i>	20
Report on Multiplex Experimental Work at WCAU-FM, <i>E. J. Meehan, Jr.</i>	27
WABC Field Test of Compatible Single-Sideband Transmission, <i>F. Marx and R. M. Morris</i>	42
Improved Compatible Single-Sideband Equipment for Standard Broadcast Service, <i>L. R. Kahn</i>	55
Stereophonic Disk Recordings	
RIAA Engineering Committee Activities with Respect to Stereophonic Disk Records (Abstract), <i>W. S. Bachman</i>	61
The Westrex Stereodisk System, <i>C. C. Davis and J. G. Frayne</i>	62
Tracing Distortion in Stereophonic Disk Recording, <i>M. S. Corrington and T. Murakami</i>	73
Compatibility Problems in Stereophonic Disk Reproduction (Abstract), <i>B. B. Bauer and R. Snepvangers</i>	82
Phonograph Pickups for Stereophonic Record Production (Abstract), <i>W. S. Bachman and B. B. Bauer</i>	83
The Requirements of a Record Changer, the Component Part and Associated Equipment for Stereophonic Record Production, <i>W. Faulkner</i>	84
Audio, Amplifier and Receiver Developments	
Distortion in Audio Phase Inverter and Driver Systems, <i>W. B. Bernard</i>	87
The CBS Compatible Stereophonic Disk (Title Only), <i>P. Goldmark, B. B. Bauer, and W. S. Bachman</i>	94
Design of a Transistorized Record-Playback Amplifier for Dictation Machine Application, <i>R. F. Fleming</i>	94
Single Tuned Transformers for Transistor Amplifiers, <i>S. H. Colodny</i>	95
Design Considerations for Transistorized Automobile Receivers, <i>R. A. Santilli</i>	118
Characteristics and Applications of Low Impedance Diodes Used as Voltage Variable Capacitors (Title Only), <i>W. F. Palmer and D. H. Rice</i>	125
Radio and Television	
Design Considerations in Transformerless Single Rectifier Television Receivers, <i>D. Sillman</i>	132
Problems in Two-Dimensional Television Systems, <i>R. M. Bowie</i>	133
On the Quality of Color Television Images and the Perception of Color Detail (Title Only), <i>O. H. Schade</i>	140
Improvements in Deflection Amplifier Design, <i>C. Droppa</i>	146
AGC Design Considerations for Television Receivers, <i>R. H. Overdeer</i>	147

Part 8—Communications, Military, Radio Frequency Interference

Vehicular Communications	
Direct Despatch Service, <i>A. J. Dinnin</i>	3
A Unique Radio System for Flood Forecasting, <i>W. C. Wray</i>	9
A New Approach to Broadband Vehicular Antennas, <i>H. Brueckmann</i>	19
Mobilization of Transistors, <i>R. E. Hansen</i>	28
Vehicular Noise Problems in Modern Land Mobile Systems (Abstract), <i>S. F. Meyer</i>	33
Techniques and Criteria Considerations in Electronic Engineering	
Use of Kros-Term System for Quick Retrieval of the Technical Detail from Large Pools of Information, <i>A. P. Vigliotta and K. D. Swartzel</i>	34
Techniques for the Presentation of Three-Dimensional Information, <i>E. J. Kennedy and E. F. LaForge</i>	44
Transistorized Airborne Military Television Techniques, <i>J. J. Kelly</i>	48
Design Criteria for Missile Automatic Test Equipment, <i>W. O. Campbell</i>	54
Active Space-Frequency Correlation Systems (Abstract), <i>W. E. Kock and J. L. Stone</i>	58
Radar in Military Electronics	
Automatic and Continuous Radar Performance Monitor, <i>W. C. Woods</i>	59
Analysis and Theoretical Investigation of New Military Electronic Missile and Aircraft-Borne Equipment, <i>D. Ehrenpreis</i>	66
Packaged High Power Radar Transceivers, <i>H. N. C. Ellis-Robinson</i>	74
Limitations of the Output Pulse Shape of High Power Pulse Transformers, <i>R. G. deBuda and J. Vilcans</i>	87
A Radar Electronic Countermeasures Simulator, <i>L. Sternlicht</i>	94
Aspects of RF Interference in Military Electronic and Communications Systems	
Treatment and Methods of Reducing Pulse and Random Interference, <i>P. M. Creutz</i>	106

Reduction of Bandwidth Requirements for Radio Relay Systems, <i>A. Mack, A. Meyerho, D. L. Jacoby, and R. H. Levine</i>	114
Analysis of the Spectral Shape of Modulation Splatter, <i>R. Price</i> ..	119
Near-Zone Power Transmission Formulas, <i>M.-K. Hu</i>	128
Radio Frequency Interference	
Bandwidth Conservation in Pulse Modulated Radars, <i>R. A. Rosien and R. Shavlach</i>	139
Measurement of Spurious Radiation from Missile-Borne Electronic Equipment, <i>A. L. Albin and C. B. Pearlston, Jr.</i>	155
Small, Lightweight RF Interference Suppressors Using Transistors, <i>W. Pecola</i>	164
Spurious Frequency Measurement in Waveguide, <i>M. Morelli</i>	176
General Communications Systems	
Digital Communication Systems, <i>R. L. Plouffe</i>	186
Constant Amplitude Speech, <i>P. J. Ferrell</i>	190
Exploitation of Physical Phenomena for Communications, <i>J. L. Ryerson</i>	192
Reduction of Intermodulation in Microwave Systems by Using Ferrite Load Isolators, <i>N. P. Weinhouse</i>	206
The Effects of Pulse Shape and Frequency Separation on FSK Transmission Through Fading, <i>G. L. Turin</i>	217
A 45 Channel PPM System, <i>S. Schreiner and B. McAdams</i>	225
New Trends in Directional Communications, <i>R. C. Benoit, Jr. and F. Coughlin, Jr.</i>	230
Long Distance Communications	
Single Channel Radioteletype Communication, <i>H. B. Voelcker, Jr.</i>	237
A World-Wide High Frequency Single Sideband Radio Network, <i>E. Bray</i>	245
Comparison of Multichannel Radioteletype Systems over a 5000-Mile Ionospheric Path, <i>A. T. Brennan, B. Goldberg, and A. Eckstein</i>	254
Basic Analysis on Controlled Carrier Operation of Tropospheric Scatter Communication Systems, <i>L. P. Yeh</i>	261
Transportable Tropospheric Scatter Communications Systems, <i>A. J. Svien and J. C. Domingue</i>	284
Evaluation of IF and Baseband Diversity Combining Receivers (Abstract), <i>R. T. Adams and B. M. Mines</i>	291
Transmission of Digital Data over Multihop Tropospheric Scatter Circuits, <i>C. N. Lawrence</i>	292
Broadcast Transmission Systems and Communications Systems	
An Expanded Theory for Signal-to-Noise Performance of FM Systems Carrying Frequency Division Multiplex, <i>D. P. Harris</i>	298
The Generation of Single-Sideband Carrier Telephone Channels by Polyphase Modulation, <i>J. R. Mensch</i>	305
Tele-Map, <i>H. Hoffmann, Jr.</i>	314

Part 9—Medical Electronics, Nuclear Science

Controlled Thermonuclear Power	
Controlled Thermonuclear Fusion—What It Means to the Radio Engineer, <i>E. W. Herold</i>	3
Hydromagnetic Stability, <i>I. B. Bernstein</i>	11
Microwave Measurements in Controlled Fusion Research, <i>M. A. Hersh</i>	14
Neutron Production in a Linear Pinch, <i>O. A. Anderson and R. V. Pyle</i>	19
Production of Intense Magnetic Fields and Their Relation to Fusion Reactors (Title Only), <i>M. Levine</i>	27
Plasma Motors, <i>W. H. Bostick</i>	28
Medical Electronics	
A New Nipkow-Disk Scanner for Accurate Cytological Measurements, <i>H. S. Sawyer and R. C. Bostrom</i>	37
Electrocardiograph Telemetering (Radio), <i>J. C. Webb, L. E. Campbell, and J. G. Hartsock</i>	43
Electronics in Biochemical Spectroscopy, <i>T. F. Gallagher and M. Rogoff</i>	50
Patient-Data Systems for Hospitals, <i>G. N. Webb and G. G. Knickerbocker</i>	58
A New Intracardiac Pressure Measuring System for Infants and Adults, <i>A. Warnick and E. H. Drake</i>	68
The Electronic Evaluation of Fetal Distress, <i>E. H. Hon</i>	74
Biological Transducers	
Panel Discussion, <i>O. H. Schmitt, S. Galler, K. Frank, K. Hartline, G. Stephens, and T. Sandel</i>	80

Part 10—Education, Writing and Speech, Management

Engineering Writing and Speech	
Roadblocks in Technical Writing, <i>T. Griggs</i>	3
Writing for a Technical Journal, <i>E. T. Ebersol, Jr.</i>	8
Nontechnical Help for Engineer-Writers, <i>R. B. MacPherson</i>	12
We Are What We Say, <i>A. Hensian</i>	17
The Automatic Creation of Literature Abstracts (Auto-Abstracts), <i>M. P. Lohu</i>	20
Planning Against Time	
Weapons Systems Development, <i>L. Fulton</i>	28
Commercial Product Development (Title Only), <i>R. Thalner</i>	33
Scientific Manpower (Title Only), <i>H. A. Meyerhoff</i>	34
Changing Demands on the Breadth of Electrical Engineering Education	
Broadening the Educational Background for Electrical Engineers, <i>S. W. Herwald</i>	35
On the Future Mathematical Curriculum for Electrical Engineers, <i>H. O. Pollak</i>	37
What Is a Broad Education Today? <i>D. B. Sinclair</i>	40
The Broadening Horizons of the Engineer, <i>G. K. Teal</i>	42

INDEX TO AUTHORS

Listings are by part number and page

A

Abbas, S. A. pt4 263
Abramson, N. pt4 22
Adams, R. T. pt8 291
Albin, A. L. pt8 155
Alessio, S. pt6 283
Anderson, B. H. pt2 199
Anderson, G. W. pt4 182
Anderson, O. A. pt9 19
Arditi, M. pt1 3
Arenberg, D. L. pt2 121
Aseltine, J. A. pt4 182
Ashbrook, J. M. pt4 94
Atti, E. pt3 3
Axelbank, M. pt2 147

B

Bachman, W. S. pt7 61; pt7 83; pt7 94
Bailey, H. A. pt6 108
Baldrige, B. H., pt5 63
Baldwin, M. W. pt4 107
Barszczewski, A. pt6 245
Batcher, R. R. pt6 294
Batsel, C. N. pt5 3
Bauer, B. B. pt7 82; pt7 83; pt7 94
Becker, C. H. pt4 255
Begun, S. J. pt5 109
Behrent, L. F. pt5 251
Bellman, R. pt4 16
Benoit, R. C., Jr. pt8 230
Bension, J. pt6 26
Berkner, L. V. pt5 258
Bernard, W. B. pt7 87
Bernstein, I. B. pt9 11
Biernson, G. A. pt4 126
Bigelow, G. F. pt5 34
Blair, G. R. pt1 48
Blattner, D. pt3 101
Blumhagen, V. A. pt6 280
Bobber, R. J. pt2 185
Bongiorno, J. J. pt2 30
Bostick, W. H. pt9 28
Bostrom, R. C. pt9 37
Bowie, R. M. pt7 140
Braun, E. L. pt4 168
Bray, E. pt8 245
Brennan, A. T. pt8 254
Bridges, J. M. pt6 314
Brooks, R. M. pt5 95
Brown, A. B. pt4 37
Brueckmann, H. pt8 19
Burfeind, R. pt5 150
Burns, J. D. pt1 133

C

Cadra, V. J. pt3 49
Campbell, L. E. pt9 43
Campbell, W. O. pt8 54
Caplan, P. J. pt1 19
Carver, T. R. pt1 3
Chadwick, G. G. pt1 213
Chang, S. S. L. pt4 79
Chapman, S. pt5 258
Cheng, D. K. pt1 152
Chestnut, H. pt4 108
Chown, J. B. pt1 199
Cicchetti, J. B. pt3 84
Clark, J. W. pt6 178
Colodny, S. H. pt7 118
Combs, T. C. pt6 34
Cooper, H. W. pt1 230
Cooter, I. L. pt5 217
Corrington, M. S. pt7 73
Cosgriff, R. L. pt1 72
Coughlin, F., Jr. pt8 230
Creutz, P. M. pt8 106
Critchlow, D. L. pt4 263
Czorny, V. pt 6 244

D

Daniels, K. B. pt2 118
Davenport, W. B. pt3 4
Davidoff, F. pt7 5
Davis, C. C. pt7 62
Davis, H. pt5 80
deBettencourt, J. T. pt1 121
deBey, L. G. pt5 204
deBuda, R. G. pt2 54; pt8 87
Dertinger, E. F. pt6 77
Dieter, F. A. pt1 19

Dinnin, A. J. pt8 3
DiToro, M. J. pt2 82
Dodington, S. H. pt5 55
Domingue, J. C. pt8 284
Drake, E. H. pt9 68
Draper, C. S. pt5 259
Dropkin, H. A. pt1 57
Droppa, O. H. pt7 147
DuHamel, R. H. pt1 139

E

Ebersol, E. T., Jr. pt10 8
Eckstein, A. pt8 254
Eddins, W. T. pt5 21
Egan, J. P. pt4 15
Ehrenpreis, D. pt8 66; pt5 167
Ellis-Robinson, H.N.C. pt8 74
Epstein, M. A. pt4 56
Eriksen, W. pt3 40

F

Faughnan, J. F. pt6 198
Faulkner, W. pt7 84
Ferber, L. W. pt4 279
Ferrell, P. J. pt8 190
Flaherty, J. M. pt1 158
Flaherty, P. pt3 77
Flelinger, B. J. pt6 137
Fleming, R. F. pt7 95
Frank, K. pt9 80
Frayne, J. G. pt7 62
Freedman, G. pt3 77
Fromm, W. E. pt1 78
Fubini, E. G. pt1 78; pt2 11
Fulton, L. pt10 28

G

Gallagher, T. F. pt9 50
Galler, S. pt9 80
Gehman, J. B. pt5 198
Goldberg, B. pt1 121; pt8 254
Goldman, H. pt3 144
Goldmark, P. pt7 94
Goode, H. H. pt4 108
Goodnow, A. C. pt7 14
Graham, R. E. pt4 100
Gray, A. R. pt6 49
Gray, L. F. pt3 114
Grayzel, A. I. pt1 91
Grever, J. L. pt7 4
Griggs, T. pt10 3
Griswold, D. M. pt3 49
Groginsky, H. L. pt4 160
Guillemin, E. A. pt2 11
Guzmann, O. pt4 217

H

Hafner, E. pt5 243
Hagens, H. H. pt6 12
Handly, E. pt3 40
Hanel, R. A. pt5 136
Haneman, W. J. pt4 254
Hansen, R. E. pt8 28
Harmon, R. N. pt7 20
Harris, D. P. pt8 298
Harris, W. P. pt5 217
Hartline, K. pt9 80
Hartsock, J. G. pt9 43
Heald, M. A. pt9 14
Henderson, K. W. pt9 235
Henesian, A. pt10 17
Henry, G. E. pt2 210
Herold, E. W. pt9 3
Herrick, J. F. pt2 199
Herwald, S. pt4 108
Herwald, S. W. pt10 35
Heyne, J. B. pt6 118
Hill, R. M. pt1 83
Hoffman, M. pt1 230
Hoffmann, H., Jr. pt8 314
Hogan, E. V. pt5 63
Hon, E. H. pt9 74
Hougardy, H. H. pt1 177
Hougardy, R. W. pt1 225
Howard, D. D. pt5 176
Hoy, W. F. pt5 95
Hu, M.-K. pt8 128
Hueter, T. F. pt2 167
Hull, J. A. pt5 228
Hunter, H. H. pt5 183
Huppert, P. A. pt6 187
Hurd, C. C. pt6 307

Hykes, G. R. pt5 131
Hyneman, R. F. pt1 225

I

Isaacson, S. pt1 230

J

Jacke, S. E. pt2 210
Jacoby, D. L. pt8 114
Jensen, H. pt6 259
Johnson, G. W. pt4 70
Johnson, R. P. pt4 108
Jolly, S. A. pt6 90
Jones, T. R. pt6 310

K

Kalaba, R. pt4 16
Kapuscienski, S. J. pt2 118
Kaufmann, P. pt3 77
Keary, T. J. pt1 127
Keen, H. S. pt1 78
Kelly, J. J. pt8 48
Kennaugh, E. M. pt1 72
Kennedy, E. J. pt8 44
Kiessling, R. C. pt2 61
Kim, W. H. pt2 76
Kirby, R. C. pt1 112
Klein, G. pt3 94
Knapp, C. F. pt4 88
Knickerbocker, C. G. pt9 58
Knox, P. C. pt10 196
Kochenburger, R. J. pt4 108
Kock, W. E. pt8 p58
Kullmann, E. V. pt5 142

L

LaForge, E. F. pt8 44
Lamphier, W. C. pt6 207
Lane, A. L. pt4 246
Lapidus, L. pt3 57
Lascaro, C. P. pt6 206
Lawrence, C. N. pt8 292
Lazzarini, R. F. pt6 108
Lea, N. pt5 234
Leaver, E. W. pt6 273
Leavitt, J. A. pt2 143
Lehmann, J. pt4 254
Lerner, R. M. pt4 27
Levi, E. pt5 216
Levine, M. pt9 27
Levine, R. H. pt8 114
Levinson, E. pt4 141
Levy, M. pt6 243; pt6 244
Lewis, H. O. pt6 223
Linville, W. K. pt4 108
Lockhart, N. F. pt4 268
Loiselle, R. E. pt6 198
Long, A. L. pt6 206
Lovell, J. A. pt6 274
Lowenschuss, O. pt4 305
Luebbert, W. F. pt4 292
Luhn, H. P. pt10 20
Lungo, A. pt6 235

M

Mack, A. pt8 114
MacPherson, R. B. pt10 12
Mahler, B. B. pt5 55
Mainberger, W. pt1 14
Malech, R. G. pt1 193
Mancini, A. R. pt4 182
Martin, J. R. pt4 255
Marx, F. pt7 42
Massa, F. pt2 210
Matthaei, G. L. pt1 98
Matthews, A. R. pt6 123
May, J. E. pt2 134
Mayeda, W. pt2 70
McAdams, B. pt8 225
McCoubrey, A. O. pt1 10
McCue, J. J. G. pt2 143
McKay, M. W. pt5 71
McMillan, S. H. pt5 26
Meehan, E. J., Jr. pt7 27
Meitzler, A. H. pt2 153
Mensch, J. R. pt8 305
Meyer, S. F. pt8 33
Meyer, W. A. pt1 200
Meyerhoff, A. pt8 114
Meyerhoff, H. A. pt10 34
Meyers, S. T. pt4 37
Mickey, L. W. pt1 213

Mindes, B. M. pt8 291
Mitchell, A. pt3 57
Mitchell, J. M. pt4 206
Montijo, R. E. pt5 3
Moore, J. pt4 108
Morcerf, F. J. pt6 3
Morelli, M. pt8 176
Morita, T. pt1 199
Morris, R. M. pt7 42
Morrow, C. W. pt1 166
Munushian, J. pt3 84
Murakami, T. pt7 73

N

Naresky, J. J. pt6 165
Neher, M. pt2 199
Nierenberg, A. pt5 150
Noden, D. A. pt4 225

O

Oates, W. L. pt6 20
Ore, F. R. pt1 139
Orenberg, A. pt1 14
Overdeer, R. H. pt7 154

P

Palevsky, M. pt4 232
Palmer, W. F. pt7 132
Papoulis, A. pt2 42; pt2 102
Pearlston, C. B., Jr. pt8 155
Pecota, W. pt8 164
Perlman, S. pt5 150
Peters, R. D. pt6 26
Peterson, R. M. pt3 21
Pierce, R. L. pt4 255
Plante, R. A. pt2 167
Plouffe, R. L. pt8 186
Pollack, L. pt3 114
Pollak, H. O. pt10 37
Popkin-Clurman, J. R. pt7 5
Post, G. pt4 168
Preist, D. H. pt3 106
Preston-Thomas, H. pt5 258
Price, R. pt8 119
Puro, W. O. pt1 200
Pyle, R. V. pt9 19

R

Raudenbush, D. H. pt5 211
Renner, G. W. pt2 167
Rice, D. H. pt7 132
Ricketts, P. E. pt5 50
Ries, F. X. pt5 251
Ritchart, R. C. pt3 21
Roehm, L. F. pt6 3
Rogoff, M. pt9 50
Root, D. pt3 77
Rosenberg, L. pt2 92
Rosien, R. A. pt8 139
Ross, I. L. pt7 12
Ross, J. D. pt2 118
Rothbart, A. pt2 92
Ruhman, S. pt4 206
Ryder, J. D. pt6 302
Ryerson, J. L. pt8 192; pt4 236

S

Sack, E. A. pt3 31
Sadler, L. S. pt7 3
Saltzman, H. pt1 240
Sandel, T. pt9 80
Sander, S. pt1 152
Santilli, R. A. pt7 125
Sardella, J. J. pt3 68
Sarture, C. W. pt4 182
Sawyer, H. S. pt3 37
Saxl, E. J. pt2 39
Schade, O. H. pt7 146
Scharfman, W. E. pt1 199
Schildknecht, R. O. pt6 186
Schmitt, O. H. pt9 80
Schreiber, W. F. pt4 88
Schreiner, S. pt8 225
Schwartz, J. W. pt3 13
Scott, W. G. pt1 200
Seely, E. W. pt1 133
Selby, M. C. pt5 251
Setrin, M. pt5 80
Sharma, R. L. pt6 223
Shavlach, R. pt8 139

Sher, N. pt1 27
 Shiffman, B. pt4 327
 Shiner, G. pt4 296
 Shipley, W. U. pt6 90
 Siebert, W. M. pt4 5
 Sillman, D. pt7 133
 Simons, D. G. pt5 258
 Sinclair, D. B. pt10 40
 Smuckler, E. J. pt5 3
 Snepvangers, R. pt7 82
 Soohoo, R. F. pt1 36
 Spanos, W. M. pt5 94
 Spittlehouse, D. pt3 77
 Spradley, J. L. pt1 204
 Stahl, P. D. pt6 152
 Stampfl, R. A. pt5 136
 Star, J. pt5 43
 Stavits, G. pt1 240
 Stedman, D. F. pt6 259
 Stephens, G. pt10 80
 Sternlicht, L. pt8 94
 Stone, J. L. pt8 58
 Strasberg, M. pt2 210
 Sutton, W. A. pt5 26

Svien, A. J. pt8 284
 Swartzel, K. D. pt8 34
 Sykes, R. A. pt2 18
 Sykes, R. P. pt4 191

T

Taylor, L. S. pt5 34
 Taylor, P. E. pt1 166
 Tellefsen, H. pt6 283
 Teltscher, E. pt5 11
 Tersoff, A. I. pt4 318
 Tetenbaum, S. J. pt1 83
 Thalner, R. pt10 33
 Thurston, R. N. pt2 109
 Tornillo, L. M. pt2 109
 Triolo, F. J. pt1 183
 Turczyn, A. pt4 246
 Turin, G. L. pt8 217

U

Ullrich, O. A. pt5 183
 Ulliyatt, K. H. pt6 259
 Unterberger, R. R. pt1 64

V

Vaccaro, F. pt3 101
 Vander Hamm, R. L. pt6 72
 Van Meter, D. pt4 3
 Van Valkenburg, M. E. pt2 70
 Vigliotta, A. P. pt8 34
 Vilcans, J. pt8 87
 Voelcker, H. B., Jr. pt8 237
 Vogelmann, J. H. pt1 84

W

Walkup, L. E. pt5 183
 Walter, C. M. pt5 107
 Ward, A. E. pt1 121
 Ward, H. T. pt1 166
 Ward, J. E. pt4 126
 Waring, W. pt3 77
 Warner, R. M., Jr. pt3 43
 Warnick, A. pt9 68
 Warren, C. S. pt4 254
 Webb, G. N. pt9 58
 Webb, J. C. pt9 43
 Webb, R. C. pt5 204
 Weil, T. A. pt5 120

Weinhouse, N. P. pt8 206
 Weisman, L. pt5 11
 Welkowitz, W. pt2 199
 Welton, K. L. pt1 133
 Wheeler, H. A. pt2 3
 Whipple, F. L. pt5 258
 Whoriskey, P. pt3 77
 Wiesner, J. B. pt5 258
 Williams, J. pt3 77
 Wing, O. pt2 48
 Winters, A. L. pt3 94
 Wirth, H. J. pt1 127
 Wolber, W. G. pt5 158
 Wonson, R. C. pt3 68
 Woods, W. C. pt8 59
 Wray, W. C. pt8 9

Y

Yaru, N. pt1 177
 Yeh, L. P. pt9 261

Z

Zimmerman, M. S. pt2 161

INDEX TO SUBJECTS

Listings are by part number and page. Authors and paper titles may be determined from the tables of contents in the front part of this index.

A

Abstracts, Literature, Automatic Creation of: pt10 20
 Acoustic Power in Industrial Ultrasonic Equipment, Measurements of: pt2 199
 Acoustic Power Radiated from Underwater Sound Transducers, Measurement of: pt2 185
 Adaptive Systems, Design of: pt4 160
 Aerographic Cathode-Ray-Tube Recorder: pt5 183
 Air Traffic Control System, Integrated Defense, Early Warning: pt5 63
 Air Traffic Control System, Vortac: pt5 50
 Airborne Digitizer, Transistorized Six-Channel: pt5 26
 Airborne Dual Antenna System for Aerial Navigation: pt5 94
 Airborne Equipment, Military Electronic Missile and: pt8 66
 Airborne Frequency Standard, Transistorized: pt5 131
 Airborne Military Television Techniques, Transistorized: pt8 48
 Airborne Vortac Distance Measuring Equipment: pt5 55
 Algebraic Decoding for a Binary Erasure Channel: pt4 56
 Ambiguity Functions, Signals with Uniform: pt4 27
 American Economy and Electronic Systems: pt6 307
 Amplifiers:
 for Automatic Control of Active DC Loads: pt6 216
 Band-Pass, Application of Piezoelectric Resonators to: pt6 235
 Deflection, Improvements in Design: pt7 147
 for Dictation Machine, Transistorized Record-Playback: pt7 95
 Feedback, with Negative Output Resistance for Magnetic Measurements: pt5 217
 Klystron, Wide Band UHF 10 KW: pt3 114
 Klystrons, Reliability in Scatter Communication Systems: pt6 108
 Linear, Drift Transistor As: pt3 49
 Maser, Two-Cavity Unilateral: pt1 27
 Transistor, Single Tuned Transformers for: pt7 118
 Amplitron and Stabilotron in MTI Radar Systems: pt5 120
 Analog Computers, Preventive Maintenance Program for Large General Purpose: pt4 191
 Analog-to-Digital Conversion Device, Solid-State: pt4 232
 Analog, Dipole Potential, Filter Synthesis in Terms of: pt2 3

Analog Rate Signal Integrator, Digital Moon-Radar Antenna Programmer with: pt4 217
 Analog-Voltage Information, Sample-and-Hold Circuits for Time Correlation of: pt5 21
 Antennas:
 Airborne Dual System for Aerial Navigation: pt5 94
 Annular Slot Direction-Finding: pt1 177
 Array, Electrically Scanned Two-Dimensional Microwave: pt1 204
 Cap-Loaded Folded: pt1 133
 Compact Dual-Purpose: pt1 200
 Directional, Remote Control of Broadcast Transmitter and: pt7 12
 Dual Beam, for Janus Doppler Navigation: pt1 240
 Early Warning Radar: pt1 158
 Helical Beam, Phase Center of: pt1 152
 Lightweight High-Gain: pt1 193
 Logarithmically Periodic: pt1 139
 Microwave, Voltage Breakdown of: pt1 199
 for Mobile UHF Relay Operation: pt1 183
 Moon-Radar, Digital Programmer with Analog Rate Signal Integrator: pt4 217
 Surface Wave, Image Line: pt1 230
 Surface-Wave, Waveguide Loaded: pt1 225
 Vehicular Broadband: pt8 19
 Apertured Plate Memory: pt4 254
 Approximation Problem in Lumped Delay Lines: pt2 102
 Arrays, Closely Spaced High Dielectric Constant Polyrod: pt1 213
 Atomic Clock, Gas Cell, Using Optical Pumping and Detection: pt1 3
 Atomic Frequency Standard, Atomichron: pt1 10; pt1 14
 Atomichron Atomic Frequency Standard: pt1 10; pt1 14
 Audio Phase Inverter and Driver Systems, Distortion in: pt7 87
 Audio and Subaudio Noise, Recording of: pt5 176
 Auto-Abstracts: pt10 20
 Automatic and Continuous Radar Performance Monitor: pt8 59
 Automatic Control Accessories, Coordinated System of: pt6 294
 Automatic Control of Active DC Loads, New Amplifiers for: pt6 216
 Automatic Creation of Literature Abstracts: pt10 20
 Automatic Gain Control Design Considerations for Television Receivers: pt7 154
 Automatic Ground Controlled Approach System: pt5 95
 Automatic Language Translator, Mark I, USAF: pt4 296

Automatic Level Control Using Vertical Interval Test Signals: pt7 5
 Automatic Soldering Machine for Printed Circuit Board Assemblies: pt6 20
 Automatic Target Detection-Position Estimation Schemes: pt5 107
 Automatic Test Equipment, Missile, Design Criteria for: pt8 54
 Automatic Transistor Classifier: pt6 3
 Automation Postal System, Canadian: pt6 243, 244, 245, 259
 Automobile Receivers, Transistorized: pt7 125

B

Backward-Wave Oscillator, Noise Characteristics of: pt3 84
 Backward-Wave Oscillator, Pulsed M-Type: pt3 94
 Band Separation Filter for 225-400 MC: pt1 91
 Bandwidth Conservation in Pulse Modulated Radars: pt8 139
 Bandwidth Requirements for Radio Relay Systems, Reduction of: pt8 114
 Baseband Diversity Combining Receivers and IF, Evaluation of: pt8 291
 Binary Erasure Channel, Algebraic Decoding for: pt4 56
 Biochemical Spectroscopy, Electronics in: pt9 50
 Biological Transducers: pt9 80
 Bridge Type Measurements, Simplified, on Quartz Crystal Units: pt5 243
 Broadcast Service, AM, Sectionalized TV Tower in: pt7 14
 Broadcast Transmitter and Directional Antenna, Remote Control of: pt7 12
 Broadcast Transmitter, Remote Controlled 50 KW: pt7 20

C

Cabinets and Cases: pt6 34
 Canadian Automation Postal System: pt6 243, 244, 245, 259
 Capacitors, Metallized, Use of: pt6 207
 Capacitors, Variable: pt7 132
 Capacitors, Voltage Variable, Low Impedance Diodes Used as: pt7 132
 Carrier Operation, Controlled, of Tropospheric Scatter Communication Systems: pt8 261
 Carrier Telephone Channels, Single-Sideband, Generation by Polyphase Modulation: pt8 305
 Cases and Cabinets: pt6 34
 Cathode-Ray-Tube Recorder, Aerographic: pt5 183
 Ceramic Coating Applications in the Electrical Field: pt6 187
 Ceramics, Ferroelectric, Power Handling Capability of: pt2 167

Channel Selection for Multicarrier Telemetry: pt5 34
 Character Sensing Equipment, Automatic Type Size Normalization in: pt4 318
 Circuits, Nonlinear, Gain-Phase Relations of: pt4 141
 Cloud Measurements, Satellite Instrumentation for: pt5 136
 Code-Marking Letters in Canadian Automation Postal System, Electrostatic Printer for: pt6 259
 Coding, Digital, TV Bandwidth Reduction by: pt4 88
 Coding and Error Checking in Canadian Automation Postal System: pt6 244
 Coil and Tape Winding, Tension in: pt6 39
 Color Television Image Quality and Perception of Color Detail: pt7 146
 Color TV Recording on Magnetic Tape: pt7 4
 Combat Computers: pt4 292
 Commercial Product Development: pt10 33
 Communication Processes Involving Learning and Random Duration: pt4 16
 Communication, Single Channel Radioteletype: pt8 237
 Communications Systems, Digital: pt8 186
 Communications Applications of Detection Theory: pt4 4
 Communications, Directional, New Trends in: pt8 230
 Communications, Exploitation of Physical Phenomena for: pt8 192
 Communications and Telemetry in Space: pt5 258
 Compatibility Problems in Stereophonic Disk Reproduction: pt7 82
 Component Part Failure Rate Analysis: pt6 72
 Component Parts and Materials, Effect of High Intensity Radiation on: pt6 206
 Component Performance, Application of Taylor's Series for Determining: pt6 118
 Components Engineer and the Sales Engineer, Partners in Reliability: pt6 196
 Components for Nuclear Radiation Environment: pt6 178
 Computers:
 Analog, Preventive Maintenance Program for Large General Purpose: pt4 191
 Balanced Precision Reference Regulator for: pt4 225
 for Canadian Automation Postal System: pt6 245
 Combat: pt4 292
 Digital, Analysis of Nonreciprocal Networks by: pt2 70
 Drum, Minimum Time Programming on: pt4 327
 Numerical Analysis of Drift Transistor Switching Times: pt3 57
 in Process Control, Systems Considerations for: pt4 168
 TRICE High Speed Incremental: pt4 206
 Constant Amplitude Speech: pt8 190
 Controlled Fusion Research, Microwave Measurements in: pt9 14
 Controlled Thermonuclear Fusion: pt9 3
 Correlation Systems, Active Space-Frequency: pt8 58
 Countermeasures, Simulator, Radar: pt8 94
 Crystal Filters, High Frequency, Design of: pt2 18
 Crystal Units, Quartz, Simplified Bridge Type Measurements on: pt5 243
 Curriculum for Electrical Engineers, On the Future Mathematical: pt10 37
 Cytological Measurements, Nipkow-Disk Scanner for: pt9 37

D

Data, Digital, Transmission, Error Correction Methods in: pt4 37
 Data, Patient-, Systems for Hospitals: pt9 58
 Decision Problem, Detection as a Statistical: pt4 3
 Decoding, Algebraic, for a Binary Erasure Channel: pt4 56
 Deflection Amplifier Design, Improvements in: pt7 147
 Delay Lines:
 Coiled Wire Torsional Wave: pt2 109
 Low-Dispersion Wired: pt2 82
 Lumped, Approximation Problem in: pt2 102
 Magnetostrictive, Transducer Networks of: pt2 92
 Temperature and Frequency Dependence of Insertion Loss in: pt2 153

Terminating Circuits, Ultrasonic: pt2 147
 Transducer Resistance, Measurement of: pt2 143
 Ultrasonic, Spurious Responses of: pt2 161
 Variable, Using Ultrasonic Surface Waves: pt2 118
 Delay, Time, Precise Measurement of: pt2 134
 Delay in Ultrasonic Systems, Measurements of: pt2 121
 Design Technique, Analytical: pt6 118
 Detection:
 Human Factors in Speech Communication in Noise: pt4 15
 Problems, Application of "Comparison of Experiments" to: pt4 22
 as a Statistical Decision Problem: pt4 3
 Theory, Applications to Radar: pt4 5
 Theory, Communications Applications of: pt4 4
 Detector, Telemetry Receiving Station Time Pulse: pt5 43
 Dictation Machine, Transistorized Record-Playback Amplifier for: pt7 95
 Digital Coding, TV Bandwidth Reduction by: pt4 88
 Digital Communication Systems: pt8 186
 Digital Computer, Analysis of Nonreciprocal Networks by: pt2 70
 Digital Computer, Numerical Analysis of Drift Transistor Switching Times: pt3 57
 Digital Data Transmission, Error Correction Methods in: pt4 37
 Digital Data Transmission over Multihop Tropospheric Scatter Circuits: pt8 292
 Digital Moon-Radar Antenna Programmer with Analog Rate Signal Integrator: pt4 217
 Digital Setting System for an X-Ray Thickness Gauge: pt6 280
 Digital Shaft Position Indicator: pt5 211
 Digitizer System of High Precision, Shaft Position: pt5 204
 Digitizer, Transistorized Six-Channel Airborne: pt5 26
 Diodes, Used as Voltage Variable Capacitors, Low Impedance: pt7 132
 Dipole Potential Analog, Filter Synthesis in Terms of: pt2 3
 Direction-Finding Antenna, Annular Slot: pt1 177
 Directional Communications, New Trends in: pt8 230
 Dispatch Service, Direct: pt8 3
 Display, ELF Electroluminescent: pt3 31
 Display and Recording Techniques, Shaped Beam: pt3 21
 Distance Measuring Equipment, Airborne Vortac: pt5 55
 Distributor Test Stand: pt6 274
 Diversity Combining Receivers, Baseband and IF, Evaluation of: pt8 291
 Doppler Navigation, Janus Type, Dual Beam Antenna for: pt1 240
 Doppler Radar Navigation System Reliability Measurements: pt6 152
 Doppler Radar Set, AN/APN 96: pt5 71
 Driving-Point Function, Non-Series-Parallel Realization of: pt2 76

E

Early Warning, Air Traffic Control System, Integrated Defense: pt5 63
 Early Warning Radar Antennas: pt1 158
 Economic Aspects of Wire Processing for Low Volume Production: pt6 26
 Economy, American, and Electronic Systems: pt6 307
 Education and Industrial Electronics: pt6 302
 Education Today, Broad: pt10 40
 Educational Background for Electrical Engineers, Broadening the: pt10 35
 Educational Needs in Systems Engineering: pt4 108
 Electrical Engineers, Broadening the Educational Background for: pt10 35
 Electrical Engineers, On the Future Mathematical Curriculum for: pt10 37
 Electrocardiograph Telemetry: pt9 43
 Electrochemical Cell for Measuring Time: pt3 40
 Electroluminescent Display, ELF: pt3 31
 Electromagnetic Scattering Problems, Impulse Response in: pt1 72
 Electron Gun, Annular Geometry: pt3 13
 Electron Tubes, Receiving, Impulse Test for Evaluating Vibrational Characteristics: pt6 90
 Electronic Evaluation of Fetal Distress: pt9 74
 Electronic Systems and the American Economy: pt6 307

Electronics in Biochemical Spectroscopy: pt9 50
 Electronics in Space Technology: pt5 259
 Electro-optical Shutter, Millimicrosecond: pt5 228
 Electrostatic Printer for Code-Marking Letters in Canadian Automation Postal System: pt6 259
 ELF Electroluminescent Display: pt3 31
 Engineer, Broadening Horizons of: pt10 42
 Engineer-Writers, Nontechnical Help for: pt10 12
 Engineers, Electrical, Broadening the Educational Background for: pt10 35
 Engineers, Electrical, On the Future Mathematical Curriculum for: pt10 37
 Error Checking and Coding in Canadian Automation Postal System: pt6 244
 Error Correction Methods in Digital Data Transmission: pt4 37
 Estiatron Electrostatically Focused Traveling-Wave Tube: pt3 101
 Exploitation of Physical Phenomena for Communications: pt8 192

F

"Facing" Machine Circuits in Canadian Automation Postal System: pt6 259
 Failure Rate Analysis, Component Part: pt6 72
 Feedback Amplifier with Negative Output Resistance for Magnetic Measurements: pt5 217
 Ferrites:
 Cores, Logic by Ordered Flux Changes in Multipath: pt4 268
 Load Isolators, Reduction of Intermodulation by: pt8 206
 Multipath Structures, Flux Patterns in: pt4 263
 Power Limiting Using: pt1 36
 Ferroelectric Ceramics, Power Handling Capability of: pt2 167
 Fetal Distress, Electronic Evaluation of: pt9 74
 Filters:
 Band Separation, for 225-400 MC: pt1 91
 Crystal, High Frequency Design: pt2 18
 Mechanical, Magnetostriction Transducers for: pt6 223
 Microwave, High Power: pt1 84
 Minimum Insertion Loss: pt2 11
 New Class of: pt2 42
 Quarter Wave Resonator, Direct-Coupled, Band-Pass: pt1 98
 Synthesis of Active RC Single-Tuned Bandpass: pt2 30
 Synthesis in Terms of Dipole Potential Analog: pt2 3
 Flight, Data System, RCA: pt5 3
 Flood Forecasting, Radio System for: pt8 9
 Fluorescent Ink in Canadian Automation Postal System: pt6 259
 Flux Patterns in Ferrite Multipath Structures: pt4 263
 Flux Responsive Magnetic Heads for Low Speed Read-Out: pt4 279
 Focused, Electrostatically, Medium-Power Traveling-Wave Tube: pt3 101
 Frequency Division Multiplex, Signal-to-Noise Performance of FM Systems Carrying: pt8 298
 Frequency-Domain Model of Linear Networks: pt4 70
 Frequency Measurement, Spurious, in Waveguide: pt8 176
 Frequency-Modulation Systems Carrying Frequency Division Multiplex, Signal-to-Noise Performance of: pt8 298
 Frequency Separation and Pulse Shape, Effect on FSK Transmission Through Fading: pt8 217
 Frequency-Shift Key Transmission Through Fading, Effects of Pulse Shape and Frequency Separation: pt8 217
 Frequency Standard, Atomichron Atomic: pt1 10; pt1 14
 Frequency Standard, Transistorized Airborne: pt5 131
 Fusion, Controlled Thermonuclear: pt9 3
 Fusion Reactors, Production of Intense Magnetic Fields and Their Relation to: pt9 27
 Fusion Research, Microwave Measurements in Controlled: pt9 14

G

Gas Cell Atomic Clock Using Optical Pumping and Detection: pt1 3

Gas Discharge Switch Tube, High Power Microwave: pt1 83
 Generation of Shaped Pulses Using Microwave Klystrons: pt3 106
 Ground Controlled Approach System, Automatic: pt5 95
 Guidance System Reliability Program, Armament: pt6 77
 Guidance Systems, Missile, Reliability of: pt6 49
 Gun, High Transconductance Wideband Television: pt3 3
 Gun, Kinescope, Annular Geometry: pt3 13

H

Helical Beam Antennas, Phase Center of: pt1 152
 Hospitals, Patient-Data Systems for: pt9 58
 Human Factors in Detection and in Speech Communication in Noise: pt4 15
 Hydromagnetic Stability: pt9 11

I

Image Quality in Color Television: pt7 146
 Imaginary Axis Translation of Transfer Functions: pt4 236
 Impulse Response in Electromagnetic Scattering Problems: pt1 72
 Impulse Test for Evaluating the Vibrational Characteristics of Receiving Tubes: pt6 90
 Inductors, Shielded Air-Cored: pt6 186
 Industrial Controls, Application of Magnetic Core Logic to: pt6 283
 Industrial Electronics:
 and Education: pt6 302
 General: pt6 273
 Help to Conserve Technical Manpower: pt6 314
 Systems: pt6 310
 Intertial Guidance System Reliability Program, Arma: pt6 77
 Information Retrieval, Kros-Term System for: pt8 34
 Insertion Loss in Delay Lines, Temperature and Frequency Dependence of: pt2 153
 Instrumentation Subjected to Severe Vibrations and Shock: pt5 167
 Instrumentation System, Multichannel: pt5 158
 Interference, Pulse and Random, Methods of Reducing: pt8 106
 Interference Suppressors, Lightweight RF, Using Transistors: pt8 164
 Interferometer, Ultraprecise Microwave: pt1 48
 Intermediate-Frequency and Baseband Diversity Combining Receivers, Evaluation of: pt8 291
 Intermodulation by Ferrite Load Isolators, Reduction of: pt8 206
 International Geophysical Year and Space Technology: pt5 258
 Interplanetary Travel and Propulsion: pt5 258
 Intracardiac Pressure Measuring System for Infants and Adults: pt9 68
 Ionosphere, Scattering, Extreme Range of VHF Transmission by: pt1 112
 Iron Lung, Servo-Pressure Control System for: pt4 126
 Isolators, Ferrite Load, Reduction of Intermodulation by: pt8 206

J

Janus Doppler Navigation Dual Beam Antenna: pt1 240

K

Kinescope Gun, Annular Geometry: pt3 13
 Klystron Amplifier, Wide Band UHF 10 KW: pt3 114
 Klystrons, Generation of Shaped Pulses Using: pt3 106
 Klystrons, Power Amplifier, Reliability in Scatter Communication Systems: pt6 108
 Kros-Term System for Retrieval of the Technical Information, Use of: pt8 34

L

Language, Automatic Translator, Mark I, USAF: pt4 296
 Learning and Random Duration, Communication Processes Involving: pt4 16
 Lenses, Microwave, Phase and Amplitude Near-Field Measurements: pt1 166
 Limiter, Video Modulation: pt7 3
 Literature Abstracts, Automatic Creation of: pt10 20
 Logic, Magnetic Core, Application to Industrial Controls: pt6 283

Logic by Ordered Flux Changes in Multipath Ferrite Cores: pt4 268

M

Magnetic Core Logic, Application to Industrial Controls: pt6 283
 Magnetic Core Matrix Switch, High Speed: pt4 246
 Magnetic Fields and Their Relation to Fusion Reactors, Production of Intense: pt9 27
 Magnetic Heads, Flux Responsive, for Low Speed Read-Out: pt4 279
 Magnetic Measurements, Feedback Amplifier with Negative Output Resistance for: pt5 217
 Magnetic Tape, Color TV Recording on: pt7 4
 Magnetography, Application to Graphic Recording: pt5 198
 Magnetography, Theory of: pt5 190
 Magnetostriction Transducers for Mechanical Filters: pt6 223
 Magnetostrictive Delay Line, Transducer Networks of: pt2 92
 Maintenance, Preventive Program for Large General Purpose Analog Computers: pt4 191
 Man in the Space Environment: pt5 258
 Manpower, Scientific: pt10 34
 Manpower, Technical, Industrial Electronics Help To Conserve: pt6 314
 Maser, Amplifier, Two-Cavity Unilateral: pt1 17
 Maser, Pulsed, Emissive Phase of: pt1 19
 Mathematical Curriculum for Electrical Engineers, On the Future: pt10 37
 Mechanical Filters, Magnetostriction Transducers for: pt6 223
 Memory, Apertured Plate: pt4 254
 Metallized Capacitors, Use of: pt6 207
 Meteor Burst Propagation: pt1 121
 Meteor Trails, Duty Cycle of Forward-Scattered Echoes from: pt1 127
 Meters, Miniature Ruggedized Precision: pt6 198
 Military Electronic Missile and Airborne Equipment: pt8 66
 Military Television Techniques, Transistorized Airborne: pt8 48
 Millimicrosecond Electro-optical Shutter: pt5 228
 Miniature Ruggedized Precision Meters: pt6 198
 Minimum Insertion Loss Filters: pt2 11
 Missile:
 and Airborne Military Electronic Equipment: pt8 66
 Automatic Test Equipment, Design Criteria for: pt8 54
 Guidance Systems, Reliability of: pt6 49
 Spurious Radiation from Equipment: pt8 155

Mobile UHF Relay Operation, Antenna for: pt1 183
 Mobilization of Transistors: pt8 28
 Modulation:
 Limiter, Video: pt7 3
 Polyphase, Generation of Single-Sideband Carrier Telephone Channels by: pt8 305
 Pulse Position, 45 Channel System: pt8 225
 Splatter, Spectral Shape of: pt8 119
 Molecular Storage and Read-Out with Microwaves: pt4 255
 Monitor, Automatic and Continuous Radar Performance: pt8 59
 Moon-Radar Digital Antenna Programmer with Analog Rate Signal Integrator: pt4 217
 Motors, Plasma: pt9 28
 Multiplex Experimental Work at WCAU-FM: pt7 27
 Multiplex, Frequency Division, Signal-to-Noise Performance of FM Systems Carrying: pt8 298

N

Navigation, Airborne Dual Antenna System for: pt5 94
 Navigation, Doppler Radar, Reliability Measurements: pt6 152
 Navigation, Janus Type Doppler, Dual Beam Antenna for: pt1 240
 Near-Zone Power Transmission Formulas: pt8 128
 Negative Output Resistance Feedback Amplifier for Magnetic Measurements: pt5 217
 Networks:
 Linear Variable, Frequency-Domain Model of: pt4 70

Nonreciprocal, Digital Computer Analysis of: pt2 70
 Topology and Signal Flow Graph: pt2 48
 Transducer, of a Magnetostrictive Delay Line: pt2 92

Neutron Production in a Linear Pinch: pt9 19
 Nipkow-Disk Scanner for Cytological Measurements: pt9 37
 Noise, Audio and Subaudio, Recording of: pt5 176
 Noise Characteristics of a Backward-Wave Oscillator: pt3 84
 Noise Problems, Vehicular, in Land Mobile Systems: pt8 33
 Nonlinear Circuits, Gain-Phase Relations of: pt4 141
 Nonreciprocal Networks, Analysis by Digital Computer: pt2 70
 Nuclear Radiation Environment, Components for: pt6 178
 Numerical Analysis on Computer, Switching Times for Drift Transistor: pt3 57

O

Optical Pumping and Detection, Gas Cell Atomic Clock Using: pt1 3
 Optical and Radar Tracking Range: pt5 142
 Oscillator, Backward-Wave, Noise Characteristics of: pt3 84
 Oscillator, Backward-Wave, Pulsed M-Type: pt3 94
 Oscillator, Quartz Servo: pt5 234

P

Packaging and Integration of Transistor Assemblies: pt6 12
 Patient-Data Systems for Hospitals: pt9 58
 Phase Inverter and Driver Systems, Audio, Distortion in: pt7 87
 Phase-Meter, Direct Reading Microwave: pt1 57
 Phonographic Pickups for Stereophonic Record Production: pt7 83
 Physical Phenomena for Communications, Exploitation of: pt8 192
 Pickups, Phonograph, for Stereophonic Record Production: pt7 83
 Piezoelectric Resonators, Application to Band-Pass Amplifiers: pt6 235
 Pinch, Linear, Neutron Production in: pt9 19
 Plasma Motors: pt9 28
 Polyphase Modulation, Generation of Single-Sideband Carrier Telephone Channels by: pt8 305
 Polyrod Arrays, Closely Spaced High Dielectric Constant: pt1 213
 Postal System, Canadian Automation: pt6 243, 244, 245, 259
 Power Limiting Using Ferrites: pt1 36
 Power Measurement, Problems in: pt2 210
 Pressure, Intracardiac, Measuring System for Infants and Adults: pt9 68
 Preventive Maintenance Program for Large General Purpose Analog Computers: pt4 191
 Printed Circuit Board Assemblies, Automatic Soldering Machine for: pt6 20
 Process Control, Systems Considerations for Computers in: pt4 168
 Product Development, Commercial: pt10 33
 Production, Low Volume, Economic Aspects of Wire Processing for: pt6 26
 Programming on a Drum Computer, Minimum Time: pt4 327
 Propulsion and Interplanetary Travel: pt5 258
 Pulses:

 Generation of Shaped, Using Microwave Klystrons: pt3 106
 Modulated Radars, Bandwidth Conservation in: pt8 139
 Position Modulation System, 45 Channel: pt8 225
 Position Telemetry System: pt5 11
 and Random Interference, Methods of Reducing: pt8 106
 Shape and Frequency Separation, Effect on FSK Transmission Through Fading: pt8 217
 Transformers, High Power, Output Pulse Shape of: pt8 87

Q

Quartz Crystal Units, Simplified Bridge Type Measurements on: pt5 243
 Quartz Servo Oscillator: pt5 234

R

Radars:
 Antennas, Early Warning: pt1 158

Applications of Detection Theory to pt4: 5
 Countermeasures Simulator: pt8 94
 Digital Moon, Antenna Programmer with Analog Rate Signal Integrator: pt4 217
 Doppler AN/APN 96: pt5 71
 Doppler Navigation System Reliability Measurements: pt6 152
 MTI, Amplitron and Stabilotron in: pt5 120
 Performance Monitor, Automatic and Continuous: pt8 59
 Pulse Modulated, Bandwidth Conservation in: pt8 139
 Signal Measurement and Recording System, High-Speed: pt5 150
 Tracking Range: pt5 142
 Transceivers, Packaged High Power: pt8 74
 Radiation, Effect of High Intensity, on Component Parts and Materials: pt6 206
 Radiation Environment, Nuclear, Components for: pt6 178
 Radiation, Spurious, from Missile-Borne Equipment: pt8 155
 Radioteletype Communication, Single Channel: pt8 237
 Radioteletype Systems, Multichannel, over a 5000-Mile Ionospheric Path: pt8 254
 Random Interference and Pulse, Methods of Reducing: pt8 106
 Reactors, Fusion, Production of Intense Magnetic Fields and Their Relation to: pt9 27
 Read-Out, Low Speed, Flux Responsive Magnetic Heads for: pt4 279
 Read-Out, Molecular Storage and, with Microwaves: pt4 255
 Receivers:
 Baseband and IF Diversity Combining, Evaluation of: pt8 291
 Television, AGC Design Considerations for: pt7 154
 Television, Transformerless Single Rectifier: pt7 133
 Transistorized Automobile: pt7 125
 Record Changer for Stereophonic Production, Requirements of: pt7 84
 Record-Playback, Transistorized Amplifier for Dictation Machine: pt7 95
 Recorder, Aerographic Cathode-Ray-Tube: pt5 183
 Recording:
 of Audio and Subaudio Noise: pt5 176
 Color TV on Magnetic Tape: pt7 4
 Graphic, Application of Magnetography to: pt5 198
 Radar-Signal: pt5 150
 Shaped Beam Techniques: pt3 21
 Stereophonic Disk, Tracing Distortion in: pt7 73
 Redundancy at Various System Levels, Reliability Improvement Through: pt6 137
 Relay Operation, Mobile UHF, Antenna for: pt1 183
 Relay Systems, Radio, Reduction of Bandwidth Requirements for: pt8 114
 Reliability:
 Improvement Through Redundancy at Various System Levels: pt6 137
 and Longevity for Space Technology: pt6 123
 Measurements, Doppler Radar Navigation System: pt6 152
 of Missile Guidance Systems: pt6 49
 Partners in, Components Engineer and the Sales Engineer: pt6 196
 of Power Amplifier Klystrons in Scatter Communication Systems: pt6 108
 Program, Arma Inertial Guidance System: pt6 77
 Results on USAF Ground Equipment: pt6 165
 Remote Control of Broadcast Transmitter and Directional Antenna: pt7 12
 Remote Controlled 50 KW Broadcast Transmitter: pt7 20
 Resonators, Piezoelectric, Application to Band-Pass Amplifiers: pt6 235
 Resonators, Quarter Wave, Direct-Coupled, Band-Pass Filters with: pt1 98
 Retrieval of the Technical Information, Kros-Term System for: pt8 34
 RF Voltmeter Calibrating Consoles: pt5 251
 Roadblocks in Technical Writing: pt10 3
 Root Square Locus Plot for Synthesizing Optimum Servo Systems: pt4 79
 Rotary Joint, Microwave: pt1 78

S

Sales Engineer and the Components Engineer, Partners in Reliability: pt6 196
 Sample-and-Hold Circuits for Time Correlation of Analog-Voltage Information: pt5 21
 Satellite Instrumentation for Cloud Measurements: pt5 136
 Scanner for Cytological Measurements, Nipkow-Disk: pt9 37
 Scanning Two-Dimensional Microwave Antenna Array, Electrically: pt1 204
 Scattering:
 Communication Systems, Reliability of Power Amplifier Klystrons in: pt6 108
 Communication Systems, Tropospheric, Controlled Carrier Operation of: pt8 261
 Communications Systems, Transportable Tropospheric: pt8 284
 Echoes from Meteor Trails, Duty Cycle of: pt1 127
 Electromagnetic Problems, Impulse Response in: pt1 72
 from Lower Ionosphere, Extreme Range of VHF Transmission by: pt1 112
 Tropospheric Multihop Circuits, Transmission of Digital Data over: pt8 292
 Scientific Manpower: pt10 34
 Self-Adjusting System for Optimum Dynamic Performance: pt4 182
 Semiconductor Component, New Passive: pt3 43
 Servo-Oscillator, Quartz: pt5 234
 Servo-Pressure Control System for Iron Lung: pt4 126
 Servo-Systems, Root Square Locus Plot for Synthesizing Optimum: pt4 79
 Shaft, Digital, Position Indicator: pt5 211
 Shaft Position Digitizer System of High Precision: pt5 204
 Shielded-Air-Cored Inductors: pt6 186
 Shock, Instrumentation Subjected to Severe Vibration and: pt5 167
 Shutter, Millimicrosecond Electro-optical: pt5 228
 Signal Flow Graph and Network Topology: pt2 48
 Signal-to-Noise Performance of FM Systems Carrying Frequency Division Multiplex: pt8 298
 Signals with Uniform Ambiguity Functions: pt4 27
 Simulator, Radar Countermeasures: pt8 94
 Single-Sideband Carrier Telephone Channels, Generation by Polyphase Modulation: pt8 305
 Single-Sideband Equipment for Standard Broadcast Service, Improved Compatible: pt7 55
 Single-Sideband Radio Network, World-Wide High Frequency: pt8 245
 Single-Sideband Transmission, WABC Field Test of Compatible: pt7 42
 Slot Direction-Finding Antenna, Annular: pt1 177
 Soldering Machine, Automatic, for Printed Circuit Board Assemblies: pt6 20
 Solid-State Analog-to-Digital Conversion Device: pt4 232
 Space:
 Communications and Telemetering in: pt5 258
 Environment, Man in: 258
 Flight, Terminal Environment in: pt5 258
 Technology, Electronics in: pt5 259
 Technology, IGV and: pt5 258
 Technology, Reliability and Longevity for: pt6 123
 Space-Frequency Correlation Systems, Active: pt8 58
 Spectral Shape of Modulation Splatter: pt8 119
 Spectrometer, Microwave Spin Resonance: pt1 64
 Spectroscopy, Biochemical, Electronics in: pt9 50
 Speech Communication in Noise, Human Factors: pt4 15
 Speech, Constant Amplitude: pt8 190
 Spin Resonance Spectrometer, Microwave: pt1 64
 Spurious Frequency Measurement in Waveguide: pt8 176
 Spurious Radiation from Missile-Borne Equipment: pt8 155
 Spurious Responses of an Ultrasonic Delay Line: pt2 161
 Stabilotron and Amplitron in MTI Radar Systems: pt5 120

Standard, Atomichron Atomic Frequency: pt1 10; pt1 14
 Standard, Transistorized Airborne Frequency: pt5 131
 Statistical Decision Problem, Detection As a: pt4 3
 Stereophonic Recording:
 CBS Compatible Disk: pt7 94
 Compatibility Problems in Disk Production: pt7 82
 Phonograph Pickups for: pt7 82
 Record Changer, Requirements: pt7 84
 RIAA Engineering Committee Activities: pt7 61
 Tracing Distortion in Disk Recording: pt7 73
 Westrex System: pt7 62
 Storage, Frame, in Television, Visual Effects of Using: pt4 107
 Subjective Experiments in Visual Communication: pt4 100
 Surface Wave Antenna, Image Line: pt1 230
 Surface Wave Antenna, Waveguide Loaded: pt1 225
 Surface Waves, Ultrasonic, Variable Delay Line Using: pt2 118
 Switch, High Speed Magnetic Core Matrix: pt4 246
 Switch Tube, High Power Microwave Gas Discharge: pt2 82
 Switching Theory, Nonbinary: pt4 305
 Switching Times, High Current, for a P-N-P Drift Transistor, Computer Analysis of: pt3 57
 Symmetry Relations, Two-Terminal Pair: pt2 61
 Synthesis of Active RC Single-Tuned Bandpass Filters: pt2 30
 System Performance, Application of Taylor's Series for Determining: pt6 118
 Systems Considerations for Computers in Process Control: pt4 168
 Systems Engineering, Educational Needs in: pt4, 108

T

Tape, Magnetic, Color TV Recording on: pt7 4
 Target Detection-Position Estimation Schemes, Automatic: pt5 107
 Taylor's Series for Determining Component and System Performance, Application of: pt6 118
 Technical Journal, Writing for: pt10 8
 Technical Writing, Roadblocks in: pt10 3
 Tele-Map: pt8 314
 Telemetering:
 Channel Selection for Multicarrier System: pt5 34
 Electrocardiograph: pt9 43
 Pulse Position System: pt5 11
 Receiving Station Time Pulse Detector: pt5 43
 in Space: pt5 258
 Telephone Channels Single-Sideband Carrier, Generation by Polyphase Modulation: pt8 305
 Television:
 Bandwidth Reduction by Digital Coding: pt4 88
 Color Image Quality and Perception of Color Detail: pt7 146
 Color Recording on Magnetic Tape: pt7 4
 Frame Storage in, Visual Effects of Using: pt4 107
 Gun, High Transconductance Wideband: pt3 3
 Receivers, AGC Design Considerations for: pt7 154
 Receivers, Transformerless Single Rectifier: pt7 133
 Sectionalized Tower in AM Broadcast Service: pt7 14
 Transistorized Airborne Military Techniques: pt8 48
 Two-Dimensional Systems: pt7 140
 Terminal Environment in Space Flight: pt5 258
 Thermonuclear Fusion, Controlled: pt9 3
 Three-Dimensional Information, Presentation of: pt8 44
 Time, Tube That Tells: pt3 40
 Topology, Network, Signal Flow Graph and: pt2 48
 Tracking Range, Optical and Radar: pt5 142
 Traffic Capacity of Transponder Systems, Increasing the: pt5 80

Transceivers, Packaged High Power Radar: pt8 74

Transducers:

Biological: pt9 80

Magnetostriction, for Mechanical Filters: pt6 223

Networks of Magnetostrictive Delay Line: pt2 92

Resistance, Delay-Line, Measurement of: pt2 143

Underwater Sound, Measurement of

Acoustic Power Radiated from: pt2 185

Transfer Functions, Imaginary Axis Translation of: pt4 236

Transformer Windings, Power, New Transpositions in: pt2 54

Transformers, Pulse, High Power Output Pulse Shape of: pt8 87

Transformers for Transistor Amplifiers, Single Tuned: pt7 118

Translator, USAF Automatic Language, Mark I: pt4 296

Transistors:

Airborne Frequency Standard: pt5 131

Airborne Military Television Techniques: pt8 48

Amplifiers, Single Tuned Transformers for: pt7 118

Assemblies, Packaging and Integration of: pt6 12

Automobile Receivers: pt7 125

Classifier, Automatic: pt6 3

Drift, High Current Switching Times, Computer Analysis of: pt3 57

Drift, As a Linear Amplifier: pt3 49

Five-Watt, Class A, Silicon Power: pt3 77

High Frequency Diffused Base N-P-N Silicon: pt3 68

Mobilization of: pt8 28

Record-Playback Amplifier for Dictation Machine: pt7 95

RF Interference Suppressors Using: pt8 164

Six-Channel Airborne Digitizer: pt5 26

Transmission Formulas, Near-Zone Power: pt8 128

Transmitter, Broadcast, Remote Control of: pt7 12

Transmitter, Remote Controlled 50 KW Broadcast: pt7 20

Transponder Systems, Increasing the Traffic Capacity of: pt5 80

Traveling-Wave Tube, Estiatron Electrostatically Focused: pt3 101

TRICE High Speed Incremental Computers: pt4 206

Tropospheric Scatter Circuits, Multihop, Transmission of Digital Data over: pt8 292

Tropospheric Scatter Communication Systems, Controlled Carrier Operation of: pt8 261

Tropospheric Scatter Communications Systems, Transportable: pt8 284

Tube That Tells Time: pt3 40

Two-Terminal Pair Symmetry Relations: pt2 61

U

Ultrasonics:

Delay Line, Spurious Responses of: pt2 161

Delay-Line Terminating Circuits and Passband Measurements: pt2 147

Equipment, Industrial, Measurements of Acoustic Power in: pt2 199

Instrument for Measuring Intensity of: pt2 189

Surface Waves, Variable Delay Line Using: pt2 118

Systems, Measurements of Delay in: pt2 121

Underwater Sound Transducers, Measurement of Acoustic Power Radiated from: pt2 185

V

Vehicular Antennas, Broadband: pt8 19

Vehicular Noise Problems in Land Mobile Systems: pt8 33

Vertical Interval Test Signals, Automatic Level Control Using: pt7 5

Vibrational Characteristics of Receiving Tubes, Impulse Test for Evaluating: pt6 90

Vibrations and Shock, Instrumentation Subjected to Severe: pt5 167

Video Modulation Limiter: pt7 3

Visual Communication, Subjective Experiments in: pt4 100

Visual Effects of Using Frame Storage in Television: pt4 107

Voltmeter Calibrating Consoles, RF: pt5 251

Vortac Air Traffic Control System: pt5 50

Vortac, Airborne, Distance Measuring Equipment: pt5 55

W

Wave Propagation, Meteor Burst: pt1 121

Waveguide-Loaded Surface-Wave Antenna: pt1 225

Waveguide, Spurious Frequency Measurement in: pt8 176

Weapons Systems Development: pt10 28

We Are What We Say: pt10 17

Westrex Stereophonic Disk System: pt7 62

Winding, Coil and Tape Tension in: pt6 39

Wire Processing for Low Volume Production, Economic Aspects of: pt6 26

Writers, Engineer, Nontechnical Help for: pt10 12

Writing for a Technical Journal: pt10 8

Writing, Technical, Roadblocks in: pt10 3

X

X-Ray Thickness Gauge, Digital Setting System for: pt6 280

1958 IRE NATIONAL CONVENTION RECORD PRICES

Part	Subject	Free to Paid Members of Following IRE Professional Groups	Prices for Members (M) Colleges and Libraries (L) Non-Members (NM)		
			M	L	NM
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Index to

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TABLE OF CONTENTS

Part 1	
Antennas and Propagation, Microwaves.....	3
Part 2	
Circuit Theory.....	3
Part 3	
Electron Devices.....	3
Part 4	
Automatic Control, Computers, Human Factors, Information Theory.....	3
Part 5	
Aeronautical, Instrumentation, Medical, Nuclear, Telemetry.....	4
Part 6	
Components, Industrial Electronics, Production, Reliability.....	4
Part 7	
Audio, Broadcast, Receivers.....	4
Part 8	
Communications, Military, Vehicular.....	5
Part 9	
Writing and Speech, Management.....	5
Index to Authors.....	5
Index to Subjects.....	6
1958 IRE Wescon Convention Record Prices.....	10

IRE WESCON CONVENTION RECORD

Contents of Volume II—1958

Part 1—Antennas and Propagation, Microwaves

Microwave Theory and Techniques I	
Mode Conversion Filters, <i>E. A. Marcatili</i>	3
Properties of the H-Guide at Microwaves and Millimeter Waves, <i>F. J. Tischer</i>	4
The Effects of Mode Conversion in Long Circular Waveguide, <i>W. D. Warters and H. E. Rowe</i>	13
A New Class of Artificial Dielectrics, <i>M.-K. Hu and D. K. Cheng</i>	21
An Accurate Frequency Measuring Technique Using Paramagnetic Resonance Phenomena in the X-Band Region, <i>P. A. Crandell</i>	26
Microwave Theory and Techniques II	
The Power Handling Capacity of Slab Lines, <i>G. M. Badoyannis</i>	35
RF Circuits for a Voltage-Tunable Magnetron, <i>W. J. Gemulla</i>	39
An S-Band Two-Phase Demodulator, <i>R. B. Wilds</i>	48
Some Notes on Strip Transmission Line and Waveguide Multiplexers, <i>D. Alstadter and E. O. Houseman, Jr.</i>	54
On the Solution of Some Microwave Problems by an Analog Computer, <i>D. M. Byck and A. Norris</i>	70
Microwave Propagation	
Forward Scatter of Electromagnetic Waves by Spheres (Abstract), <i>W. E. Kock, J. L. Stone, J. E. Clark, and W. D. Friedle</i>	86
Propagation Through Random Distributions of Spheres, <i>C. I. Beard and V. Twersky</i>	87
Surface Waves on a Right-Angled Wedge, <i>S. N. Karp and P. C. Karal, Jr.</i>	101
New Concepts in the Statistical Study of Tropospheric Scatter Propagation Data, <i>L. P. Yeh</i>	104
Microwave Ferrites	
Circular Electric Waves Propagating Through the Circular Waveguide Containing a Circumferentially Magnetized Ferrite Cylinder, <i>N. Kumagai and K. Takeuchi</i>	123
A Wide-Band Nonreciprocal TEM-Transmission-Line Network, <i>E. M. T. Jones, S. B. Cohn, and J. K. Shimizu</i>	131
Field Displacement Effects in Dielectric and Ferrite Loaded Waveguides, <i>T. M. Straus</i>	135
Experimental Techniques in Measuring Ferrite Line Widths With a Cross-Guide Coupler, <i>D. C. Stinson</i>	147
Tee Circulator, <i>W. E. Swanson and G. J. Wheeler</i>	151
Antenna Arrays	
Arbitrarily Polarized Slot Array, <i>H. H. Hougardy and H. E. Shanks</i>	157
Logarithmically Periodic Antenna Arrays, <i>R. H. DuHamel and D. G. Berry</i>	161
Impedance Properties of Antenna Arrays, <i>S. Edelberg and A. A. Oliner</i>	175
Antenna Pattern Synthesis of the Most Truthful Approximation, <i>H. P. Raabe</i>	178
A Rapid-Scanning Phased Array for Propagation Measurements, <i>R. E. Miller, A. T. Waterman, Jr., G. K. Dufey, and W. H. Huntley, Jr.</i>	184
Antennas and Propagation	
The Influence of Radar Reflection Characteristics of the Moon on Specifications for Earth-Moon-Earth Communication Systems, <i>T. B. A. Senior, K. M. Siegel, and H. Weil</i>	197
A Microwave Technique To Reduce Platform Motion and Scanning Noise in Airborne Moving-Target Radar, <i>D. B. Anderson</i>	202
A Concentric Loop Array, <i>A. C. Schell and E. L. Bouché</i>	212
Theory and Design of a Class of Luneberg Lenses, <i>J. R. Huynen</i>	219
Obstacle Gain at Microwave Frequencies, <i>S. R. Bradshaw</i>	231
Antennas	
A Broadband, Low Sidelobe, Radar Antenna, <i>A. M. McCoy, J. E. Walsh, and C. F. Winter</i>	243
A Class of Low Gain Broadband Antennas, <i>B. J. Lamberty</i>	251
Illuminating Curved Passive Reflector With Defocused Parabolic Antenna, <i>R. F. H. Yang</i>	260
Reflector-Type Periodic Broadband Antennas, <i>R. E. Franks and C. T. Elfving</i>	266
The Parabolic Dome Antenna: A Large Aperture, 360 Degree, Rapid Scan Antenna, <i>J. D. Barab, J. G. Marangoni, and W. G. Scott</i>	272

Part 2—Circuit Theory

Circuit Analysis and Design	
On Topological Synthesis, <i>M. E. Van Valkenburg</i>	3
Predistorted Filter Design With a Digital Computer, <i>P. R. Geffe</i>	10
The Design of Two-Section Symmetrical Zobel Filters for Tchebycheff Insertion Loss, <i>W. N. Tuttle</i>	23
Modern Network Theory Design of Single-Sideband Crystal Filters (Abstract), <i>M. Dishal</i>	33
Transmission Through a Linear Network Containing a Periodically Operated Switch, <i>C. A. Desoer</i>	34
Circuit Design	
Graphical Interpretations for Frequency Transformations, <i>J. L. Stewart</i>	42
Optimum Synthesis of RC Ladder Networks (Abstract), <i>A. Paige and E. S. Kuh</i>	46

A New Design Method for Coupling Networks, With Applications to Broadband Transistor Amplifiers and Antenna Matching, <i>P. A. Ligomenides</i>	47
Some Developmental Techniques Concerning Distributed Amplifiers and Virtual Delay Lines, <i>W. J. Judge</i>	62
The Synthesis of Multichannel Amplifiers, <i>B. F. Barton</i>	69
Transistor Circuits	
A Wide-Range Junction Transistor Audio Oscillator, <i>M. A. Melehy</i>	74
Comparisons Between Multiple Loop and Single Loop Transistor Feedback Amplifiers, <i>E. M. Davis, Jr.</i>	78
The Root Locus Design of Transistor Feedback Amplifiers, <i>D. O. Pederson and M. S. Ghausi</i>	87
Techniques for Stabilizing DC Transistor Amplifiers, <i>M. L. Klein</i>	94
"Squared" Input Stages for Low-Level Transistor Amplifiers, <i>K. Hinrichs and B. B. Weekes</i>	104

Part 3—Electron Devices

Parametric Amplifiers and Masers	
Masers and Parametric Amplifiers, <i>H. Heffner</i>	3
Modified Semistatic Ferrite Amplifier, <i>A. D. Berk, L. Kleinman, and C. E. Nelson</i>	9
Parametric Electron Beam Amplifiers, <i>A. Ashkin, T. J. Bridges, W. H. Louisell, and C. F. Quate</i>	11
A Parametric Amplifier Using Lower-Frequency Pumping, <i>K. K. N. Chang and S. Bloom</i>	23
Solid-State Maser Systems (Abstract), <i>S. H. Autler, R. H. Kingston, A. L. McWhorter, and J. W. Meyer</i>	28
Slow-Wave Structures for Unilateral Solid-State Maser Amplifiers, <i>R. W. DeGrasse</i>	29
Microwave and High Power Tubes	
A New Design Approach for a Compact Kilowatt UHF Beam Power Tube, <i>F. W. Peterson</i>	36
A Low Voltage Helix Type Backward Wave Oscillator With Extended Tuning Range, <i>L. Maninger</i>	42
Are Klystron Amplifiers Inherently Noisy? <i>R. G. Rockwell</i>	55
A New Crossed-Field Traveling-Wave Tube, the M-J Tube, <i>C. C. Johnson and C. K. Birdsall</i>	60
Design of Traveling-Wave Tubes for Airborne Applications, <i>M. Nowogrodski</i>	66
Special Electron Devices	
Voltage-Sensitive Semiconductor Capacitors, <i>M. E. McMahon and G. F. Straube</i>	72
The Hall Effect Circulator—A Passive Transmission Device, <i>W. J. Grubbs</i>	83
Stacked Tubes in Glass Envelopes, <i>C. F. Douglass</i>	94
A Lightweight Kilowatt Klystron Amplifier for Aerial Navigation Systems in X Band, <i>R. G. Rockwell</i>	100
Characteristics and Control of Gas Tube Duplexers During Their Recovery Time, <i>R. E. Hovda and E. R. Roehl</i>	105
Solid State I	
A Family of Diffused-Base Germanium Transistors, <i>H. E. Talley</i>	115
Millimicrosecond Diffused Silicon Computer Diodes, <i>J. H. Forster and P. Zuk</i>	122
Diode Recovery Time Measurements in the Millimicrosecond Region (Abstract), <i>A. E. Bakanowski</i>	131
The Design and Characteristics of a Diffused Silicon Logic Amplifier Transistor, <i>L. E. Miller</i>	132
Switching Time Calculations for Diffused Base Transistors, <i>V. H. Grinich and R. M. Noyce</i>	141
Solid State II	
Comparison of Neutron Damage in Germanium and Silicon Transistors, <i>J. W. Easley</i>	148
High Power Silicon Transistors, <i>H. W. Henkels and T. P. Nowalk</i>	157
A Medium Power Silicon Controlled Rectifier, <i>D. K. Bisson</i>	166
PNR-N Switches, <i>J. A. Hoerni and R. N. Noyce</i>	172
A New Diode for Switching and Oscillator (Abstract), <i>L. Esaki</i>	176

Part 4—Automatic Control, Computers, Human Factors, Information Theory

Computer Applications	
Data Preparation for Numerical Control of Machine Tools, <i>H. D. Huskey and D. E. Trumbo</i>	3
A Library of Blip Samples for Use in the Realistic Simulation and Evaluation of Automatic Radar Data Processing Systems, <i>C. M. Walter and H. M. Willett</i>	8
GCA by Automatic Voice Data Link, <i>J. J. Fling and M. H. Nothman</i>	28
A Computer Simulation Chain for Research on Picture Coding, <i>R. E. Graham and J. L. Kelly, Jr.</i>	41
Mapping Vacuum Tube Computers in Transistor Circuits (Abstract), <i>G. R. Monroe and H. G. Jones</i>	47
Computer Devices	
Achieving Maximum Pulse Packing Densities and Transfer Rates, <i>B. W. Thompson and D. F. Eldridge</i>	48

An Emitter-Follower-Coupled, High-Speed Binary Counter, <i>I. Horn</i>	54
Coincident Current Applications of Ferrite Apertured Plates, <i>W. G. Rumble and C. S. Warren</i>	62
Information Storage in Microspace (Abstract), <i>S. P. Newberry</i>	66
Analog Computers	
Anticipatory Display Design Through the Use of an Analog Computer, <i>L. J. Fogel and M. Dwonczyk</i>	67
A Transistorized, All-Electronic Cosine Sine Function Generator, <i>H. Schmid</i>	89
An Analog Memory, <i>W. S. Kozak</i>	108
Network Solution of the Right Triangle Problem, <i>M. R. Winkler</i>	123
Information Theory	
The Prediction of Derivatives of Polynomial Signals in Additive Stationary Noise, <i>I. Kanter</i>	131
Predictive Quantizing of Television Signals, <i>R. E. Graham</i>	147
Optimum Linear Estimation for Random Processes as the Limit of Estimates Based on Sampled Data, <i>P. Swerling</i>	158
Random Function Probability Distributions After a Nonlinear Filter, <i>G. O. Young</i>	164
Statistical Invariance of Noise in Sampled-Data Systems, <i>S. A. Zadoff</i>	173
Automatic Control	
Compensation of Multiloop Control Systems, <i>D. Lebell and M. Mandel</i>	177
Optimization of Compensation for Cascaded Actuators in a Common Feedback Loop, <i>G. S. Axelby and E. F. Osborne</i>	182
Some Simplifying Additions to Basic Sampled-Data Theory, <i>C. O. Carlson</i>	197
Contributions to the Analysis of Nonlinear Feedback Control Systems, <i>S. L. Mikhail</i>	233
Enhanced Real-Time Data Accuracy for Instrumentation Radars by Use of Digital-Hydraulic Servos, <i>R. P. Cheetham and W. A. Mülle</i>	239
Human Factors in Engineering	
A Review and Summary of Tracking Research Applied to the Description of Human Dynamic Response, <i>D. T. McRuer and E. S. Krendel</i>	254
Synthesis of a Linear Quasi Transfer Function for the Operator in Man-Machine Systems, <i>A. S. Jackson</i>	263
The Optimization of Man-Machine Control Systems, <i>H. P. Birmingham</i>	272
Sibyl: A Laboratory for Simulation Studies of Man-Machine Systems, <i>H. D. Irvin</i>	277
Simulation of a Human Tracking Problem on the UDEC III Computer, <i>H. L. Platzer</i>	286

Part 5—Aeronautical, Instrumentation, Medical, Nuclear, Telemetry

Telemetry	
Theoretical Data Acquisition Analysis and Practical Appraisal of Existing Airborne Systems, <i>B. M. Gordon and R. D. Jorup</i>	3
A Compatible PCM/FM System (Abstract), <i>P. E. Bennewitz and H. B. Barling</i>	4
A PAM/PDM Demultiplexer With Improved Synchronization in Presence of Noise, <i>E. D. Heberling and J. M. Sacks</i>	5
Transistor Airborne PDM System, <i>W. P. Klemens</i>	13
High Acceleration Telemetry, <i>T. D. Horning</i>	20
Airborne Electronic Devices	
Broadband Radio Interference Generated by Airborne Electronic Devices Utilizing Diode Rectifiers, <i>J. C. Senn</i>	25
A Compact L-Band RF Unit for an Air Traffic Control Transponder, <i>R. C. Skar</i>	34
A Precision Digital Data Acquisition System for Instrumentation Radars, <i>R. L. Snyder</i>	41
Earth Rate Directional Reference, <i>N. Feldman</i>	54
A Digital Computer System for Terminal Area Air Traffic Control (Abstract), <i>E. L. Braun and A. S. Gianopoulos</i>	61
A Modern Approach and Landing System (ALS), <i>B. Cutler</i>	62
Instrument Tools	
Millimicrosecond Kerr Cell Camera Shutter (Abstract), <i>A. M. Zarem, F. R. Marshall, and S. M. Hauser</i>	76
A Precision Delayed Pulse Generator as a Variable Time Interval Standard, <i>D. Broderick, D. Hartke, and M. Willrodt</i>	77
Development of a Transistorized Voltage Controllable Frequency Source, <i>W. E. Wilke and W. B. Sander</i>	86
Broadband Stabilized Microwave Generators, <i>J. A. Huie and L. C. Eisaman</i>	98
Operational Feedback in Data Processing Amplifiers, <i>R. A. Smith and S. Sem-Sandberg</i>	103
Broadband Waveguide Bolometer Mounts, <i>L. I. Kent</i>	114
Industry Looks at Fusion Power	
Electrical Power Problems in Fusion Research, <i>H. Hurwitz, Jr.</i>	126
Spectroscopy Aspects of High-Temperature Fusion Research (Title Only), <i>S. Cunningham</i>	139
Ultrahigh Vacuum Research in Support of the Thermonuclear Fusion Power Program, <i>W. J. Lange</i>	140
Instrument Systems	
Space and High Vacuum, <i>J. R. Hafstrom</i>	147
Drone Tracking System With Lightweight Airborne Package, <i>E. J. Walcek</i>	151
An Automatic Telemetering Meteorological Observation System, <i>P. F. Boulay, B. I. Florey, V. R. Latorre, and M. H. Wittmeyer</i>	158
Digital Airborne Tape Recording, <i>T. Arcand, S. G. Cohen, and J. Lebid</i>	168
An Electronic Framing Camera for Millimicrosecond Photography, <i>G. L. Clark</i>	189

Measurement in Space Travel	
The Dynamic Survival Potential in Manned Space Operations, <i>D. Flickinger</i>	196
Survival and Performance of Man in Space, <i>B. H. Levedahl</i>	198
Performance—Assessing Human Capability in Space, <i>A. W. Helherington</i>	202
State of Art in Measurement (Title Only), <i>W. Young</i>	205
Future Instrumentation Problems (Title Only), <i>F. W. Lehan</i>	205
Medical Electronics	
The Design of Electronic Correlating Equipment To Be Used in Medical Research, <i>L. M. Kaplan</i>	206
Electronic Aids to the Service of Obstetrics: Electrohysterography and Fetal Electrocardiography, <i>S. D. Larks</i>	216
A Servomechanism for Automatic Regulation of Breathing, <i>G. H. Meyers and G. A. Saxton, Jr.</i>	224
Fetal Heart Rate Measurements, <i>W. E. Tolles and L. M. Hellman</i>	231

Part 6—Components, Industrial Electronics, Production, Reliability

Reliability I	
Design Techniques for Upgrading the Reliability of Weapon Systems During Flight-Readiness Checkout, <i>M. Patterson</i>	3
Reliability and Engineering Colleges, <i>C. A. Krohn</i>	10
The Confidence That Can Be Placed on Various Reliability Tests, <i>C. M. Ryerson</i>	14
Optimum Design for Reliability, the Group Redundancy Approach, <i>J. H. S. Chin</i>	23
Integrating Reliability Considerations Into Systems Analysis, <i>J. B. Heyne</i>	30
Reliability II	
Contract Implications of Military Electronics Reliability Requirements, <i>J. Allen, H. Powell, L. Arndt, and J. S. Lambert</i>	32
Improved Component Materials	
Advances in Ceramic Components, <i>H. M. Schlicke</i>	36
Monolithic Structure—A New Concept for Ceramic Capacitors, <i>J. H. Fabricius</i>	45
Up-Grading Tantalytic Capacitors, <i>W. R. Roberts</i>	52
The Thermally Fused Metal-to-Ceramic Vamistor, <i>R. C. Langford</i>	60
Factors Affecting the Formation of Deposited Carbon Film Resistors, <i>E. I. Doucette</i>	71
Component Parts	
A Discussion of the Sampling Versus Rating Dilemma on Components, <i>B. Hecht</i>	81
Design and Performance of Static-Magnetic Regulated DC Power Supplies, <i>J. T. Keefe</i>	87
ADC Reference Voltage, <i>K. Worcester</i>	104
Dynamic Temperature Coefficient Measurement, <i>A. S. Takacs and F. E. Baron</i>	111
The Development of 500°C Low-Loss High-Frequency Cables, <i>E. T. Pfund, Jr. and B. Suverkrop</i>	121
Production Techniques	
A Fresh Approach to Modular Packaging for Ground Based Data Processing Equipment, <i>C. W. Watt and N. Keefe</i>	135
Insulated Flexible Printed Circuits, <i>W. B. Wilkens</i>	141
Design and Semiautomatic Production of Stacked Ceramic Receiving Tubes, <i>R. H. Chamberlain</i>	157
Honeycomb Structure Rigidizes Printed Wiring for High Vibration, <i>E. O. Deimel</i>	166
New Organic Coatings for the Protection of Printed Circuits Under Environmental Conditions, <i>E. Harmon, J. Heffernan, and J. Staller</i>	169
Industrial Electronics	
A Numerical Control System for a Drivmatic Riveter, <i>R. D. Borsos and H. M. Lakin</i>	170
A High Performance 500 Megacycle Multistage Amplifier, <i>M. W. Hamilton and J. W. Rush</i>	177
Transistorized Decade Counter, <i>A. Szerlip</i>	181
Some Digital Industrial Electronic Systems and Their Military Heritages, <i>D. E. Wassall</i>	188
Thermal Considerations in Regulated Power Supply Design, <i>R. Wilman</i>	191

Part 7—Audio, Broadcast, Receivers

Audio	
Description and Results of Experiments With Speech Using Digital Computer Simulation, <i>E. E. David, Jr., M. V. Mathews, and H. S. McDaniels</i>	3
A Survey of Speech Bandwidth Compression Techniques (Abstract), <i>S. J. Campanella</i>	11
The Four-Track Stereotape Magazine for Home Hi-Fi, <i>R. J. Tinkhan</i>	12
A Versatile Compressor-Limiter Audio Amplifier for Studio Use, <i>E. W. Tompkin</i>	19
Research and Development on the Piano (Abstract), <i>J. P. Quiller</i>	27
Radio and Television Broadcasting	
Field Experience With the Kahn Compatible Single-Sideband System Installed at KDKA, Pittsburgh, Pennsylvania, <i>R. N. Harmon</i>	28
Head Drum Stabilization for Recording the NTSC Color Signal, <i>L. J. Kabbell</i>	29
Frequency Measurements in the Broadcast Field, <i>C. A. Cady and W. P. Buuck</i>	38
Remote Control and Automatic Logging of AM, FM, and TV Broadcasting Transmitters and Automatic Programming of AM and FM Broadcasting Stations, <i>P. C. Schafer</i>	42

Automatic Operation of Video Tape Equipment at NBC, Burbank, R. W. Byloff.....	43
Advanced Television Techniques	
Rapid Alignment Techniques for Critical Bandpass Circuitry, W. A. Sebastian.....	51
A Transistorized Television Receiver, R. R. Webster.....	57
Design and Use of the Chroma Key (Abstract), F. J. Gaskins.....	64
Distortion Reduction in TV Reception, J. Ruston and W. J. Judge.....	65

Application of Automatic Level Control in Tropospheric SSB Communication Systems, A. J. Vadasz.....	69
Personal Signaling, A New Telephone Service, N. Monk and E. D. Guernsey.....	76

Part 8—Communications, Military, Vehicular

Military Electronics	
Economic Analysis in Long Term Planning of Military Communications Systems, R. Krzyczkowski.....	
Will Timing Systems Become Heterogeneous or Homogeneous? D. R. Proctor.....	3
Automatic Missile Systems Test Considerations, J. I. Davis.....	14
Frequency Multiplex Doppler Radar, J. Galejs.....	22
Talos Land Based System Digital Checkout Equipment, F. X. Beck.....	34
Communications Systems and Vehicular Communications	
A Method of Improving Reception in FM Communications, H. D. Hern and M. S. Ulsiad.....	42
Effective Split-Channel Utilization—A Challenge to the Communication Systems Engineer, C. J. Schultz.....	46
A Double Sideband-Suppressed Carrier Communication System for Telephone Application, J. W. Halina.....	53

Part 9—Writing and Speech, Management

Modern Management Problems	
Minimizing Employee Losses When R and D Operations Relocate, R. F. Lander.....	3
Industry's New Role in Education, J. Cryden.....	7
The Sales Engineer—Human "Catalyst" of the Electronics Industry, H. A. Young.....	11
Project Direction in the Development of Avionics Systems, C. J. Godwin.....	13
Does the Present Cost-Plus-Fixed-Fee Contract Give the Government the Best Deal? B. Dempster.....	16
Project Management—Air Frame and Electronics Viewpoints	
Panel Discussion, E. N. Hall, G. Stoner, O. T. Simpson, and R. L. Shetter.....	23
Engineering Writing and Speech	
Publications and the Project Organization, M. H. Lowe.....	26
A Two-Hour Course in Report Writing, R. E. Hohmann.....	30
Should Slides Be Used in a Technical Presentation? C. L. Lillo.....	35
Making the Mathematical Equation an Effective Communication Tool, M. Hollander and E. J. Podell.....	41
A Multipurpose, Multiaudience Speech Kit, I. Seligsohn.....	50

INDEX TO AUTHORS

A	
Allen, J. pt6 32	
Alstadter, D., Jr. pt1 54	
Anderson, D. B. pt1 202	
Arcand, A. T. pt5 168	
Arndt, L. pt6 32	
Ashkin, A. pt3 13	
Autler, S. H. pt3 28	
Axelby, G. S. pt4 182	
B	
Bakoyannis, G. M. pt1 35	
Bakanowski, A. E. pt3 131	
Barab, J. D. pt1 272	
Barling, H. B. pt5 4	
Baron, F. E. pt6 111	
Barton, B. F. pt2 69	
Beard, C. I. pt1 87	
Beck, F. X. pt8 42	
Bennewitz, P. E. pt5 4	
Berk, A. D. pt3 9	
Berry, D. G. pt1 161	
Birdsall, C. K. pt3 60	
Birmingham, H. P. pt4 272	
Bisson, D. K. pt3 166	
Bloom, S. pt3 23	
Borsos, R. D. pt6 170	
Bouché, E. L. pt1 212	
Boulay, P. F. pt5 158	
Bradshaw, S. R. pt1 231	
Braun, E. L. pt5 61	
Bridges, T. J. pt3 13	
Broderick, D. pt5 77	
Buuck, W. P. pt7 38	
Byck, D. M. pt1 70	
Byloff, R. W. pt7 43	
C	
Cady, C. A. pt7 38	
Campanella, S. J. pt7 11	
Carlson, G. O. pt4 197	
Chamberlain, R. H. pt6 157	
Chang, K. K. N. pt3 23	
Cheetham, R. P. pt4 239	
Cheng, D. K. pt1 21	
Chin, J. H. S. pt6 23	
Clark, G. L. pt5 189	
Clark, J. E. pt1 86	
Cohen, S. G. pt5 168	
Cohn, S. B. pt1 131	
Crandell, P. A. pt1 26	
Cryden, J. pt9 7	
Cunningham, S. pt5 139	
Cutler, B. pt5 62	
D	
David, E. E., Jr. pt7 3	
Davis, E. M., Jr. pt2 78	
Davis, J. I. pt8 22	
DeGrasse, R. W. pt3 29	
Deimel, E. O. pt6 166	
Dempster, B. pt9 16	
Desoer, C. A. pt2 34	
Dishal, M. pt2 33	
Doucette, E. I. pt6 71	
Douglass, C. F. pt3 94	
DuHamel, R. H. pt1 161	
Durfee, G. K. pt1 184	
Dwoneczyk, M. pt4 67	
E	
Easley, J. W. pt3 148	
Edelberg, S. pt1 175	
Eisaman, L. C. pt5 98	
Eldridge, D. F. pt4 48	
Elfvig, C. T. pt1 266	
Esaki, L. pt3 176	
F	
Fabricius, J. H. pt6 45	
Feldman, N. pt5 54	
Flickinger, D. pt5 196	
Fling, J. J. pt4 28	
Florey, B. I. pt5 158	
Fogel, L. J. pt4 67	
Forster, J. H. pt3 122	
Franks, R. E. pt1 266	
Friedle, W. D. pt1 86	
G	
Galejs, J. pt8 34	
Gaskins, F. J. pt7 64	
Ge'e, P. R. pt2 10	
Gemulla, W. J. pt1 39	
Ghausi, M. S. pt2 87	
Gianoplus, A. S. pt5 61	
Godwin, C. J. pt9 13	
Gordon, B. M. pt5 3	
Graham, R. E. pt4 41; 147	
Grinich, V. H. pt3 141	
Grubbs, W. J. pt3 83	
Guernsey, E. D. pt8 76	
H	
Hafstrom, J. R. pt5 147	
Halina, J. W. pt8 61	
Hall, E. N. pt9 23	
Hamilton, M. W. pt6 177	
Harmon, E. pt6 169	
Harmon, R. N. pt7 28	
Hartke, S. pt5 77	
Hauser, S. M. pt5 76	
Heberling, E. D. pt5 5	
Hecht, B. pt6 81	
Hefner, J. pt6 169	
Hefner, H. pt3 3	
Hellman, L. M. pt5 231	
Henkels, H. W. pt3 157	
Hern, H. D. pt8 46	
Hetherington, A. W. pt5 202	
Heyne, J. B. pt6 30	
Hinrichs, K. pt2 104	
Hoerni, J. A. pt3 172	
Hohmann, R. E. pt9 30	
Hollander, M. pt9 41	
Horn, I. pt4 54	
Horning, T. D. pt5 20	
Hougardy, H. H. pt1 157	
Houseman, E. O., Jr. pt1 54	
Hovda, R. E. pt3 105	
Huie, J. A. pt5 98	
Huntley, W. H., Jr. pt1 184	
Hurwitz, H., Jr. pt5 126	
Huskey, H. D. pt4 3	
Huynen, J. R. pt1 219	
I	
Irvin, H. D. pt4 277	
J	
Jackson, A. S. pt4 263	
Johnson, C. C. pt3 60	
Jones, E. M. T. pt1 131	
Jones, H. G. pt4 47	
Jorup, R. D. pt5 3	
Judge, W. J. pt2 62; pt7 65	
K	
Kabell, L. J. pt7 29	
Kanter, I. pt4 131	
Kaplan, L. M. pt5 206	
Karal, F. C., Jr. pt1 101	
Karp, S. N. pt1 101	
Keefe, J. T. pt6 87	
Keefe, N. pt6 135	
Kelly, J. L., Jr. pt4 41	
Kent, L. I. pt5 114	
Kingston, R. H. pt3 28	
Klein, M. L. pt2 94	
Klemens, W. P. pt5 13	
Kock, W. E. pt1 86	
Kozak, W. S. pt4 108	
Krendel, E. S. pt4 254	
Krohn, C. A. pt6 10	
Krzyczkowski, R. pt8 3	
Kuh, E. S. pt2 46	
Kumagai, N. pt1 123	
L	
Lakin, H. M. pt6 170	
Lambert, J. S. pt6 32	
Lamberty, B. J. pt1 251	
Lander, R. F. pt9 3	
Lange, W. J. pt5 140	
Langford, R. C. pt6 60	
Larks, S. D. pt5 216	
Latorre, V. R. pt5 158	
Leblid, D. pt4 177	
Lebid, J. pt5 168	
Lehan, F. W. pt5 205	
Leinman, K. pt3 9	
Levedahl, B. H. pt5 198	
Ligomenides, P. A. pt2 47	
Lillo, C. L. pt9 35	
Louisell, W. H. pt3 13	
Lowe, M. H. pt9 26	
M	
Mandel, M. pt4 177	
Maninger, L. pt3 42	
Marangoni, J. G. pt1 272	
Marcatili, E. A. pt1 3	
Marshall, F. R. pt5 76	
Mathews, M. V. pt7 3	
McCoy, A. M. pt1 243	
McDonals, H. S. pt7 3	
McMahon, M. E. pt3 72	
McRuer, D. T. pt4 254	
McWhorter, A. L. pt3 28	
Melehy, M. A. pt2 74	
Meyer, J. W. pt3 28	
Meyers, G. H. pt5 224	
Mikhail, S. L. pt4 233	
Miller, L. E. pt3 132	
Miller, R. E. pt1 184	
Ming-Kuei Hu pt1 21	
Monk, N. pt8 76	
Monroe, G. R. pt4 47	
Mulle, W. A. pt4 239	
N	
Nelson, C. E. pt3 9	
Newberry, S. P. pt4 66	
Norris, A. pt1 70	
Nothman, M. H. pt4 28	
Nowalk, T. P. pt3 157	
Nowogrodski, M. pt3 66	
Noyce, R. N. pt3 141; 172	
O	
Oliner, A. A. pt1 175	
Osborne, E. F. pt4 182	
P	
Paige, A. pt2 46	
Patterson, M. pt6 3	
Pederson, D. O. pt2 87	
Peterson, F. W. pt3 36	
Pfund, T., Jr. pt6 121	
Platzner, H. L. pt4 286	
Podell, E. J. pt9 41	
Powell, H. pt6 32	
Procter, D. R. pt8 14	
Q	
Quate, C. F. pt3 13	
Quitter, J. P. pt7 27	
R	
Raabe, H. P. pt1 178	
Roberts, W. H. pt6 52	

Rockwell, R. G. pt3 55; 100
Roehl, E. R. pt3 105
Rowe, H. E. pt1 13
Rumble, W. G. pt4 62
Rush, J. W. pt6 177
Ruston, K. J. pt7 65
Ryerson, C. M. pt6 14

S

Sacks, J. M. pt5 5
Sander, W. B. pt5 86
Saxton, G. A., Jr. pt5 224
Schafer, P. C. pt7 42
Schell, A. C. pt1 212
Schlicke, H. M. pt6 36
Schmid, H. pt4 89
Schultz, C. J. pt8 53
Scott, W. G. pt1 272
Sebastian, W. A. pt7 51
Seligsohn, I. pt9 50
Sem-Sandberg, S. pt5 103
Senior, T. B. A. pt1 197
Senn, J. C. pt5 25
Shanks, H. E. pt1 157
Shetler, R. L. pt9 23

Shimizu, J. K. pt1 131
Siegel, K. M. pt1 197
Simpson, O. T. pt9 23
Skar, R. C. pt5 34
Smith, R. A. pt5 103
Snyder, R. L. pt5 41
Staller, J. pt6 169
Stewart, J. L. pt2 42
Stinson, D. C. pt1 147
Stone, J. L. pt1 86
Stoner, G. pt9 23
Straube, G. F. pt3 72
Straus, T. M. pt1 135
Suverkrop, B. pt6 121
Swanson, W. E. pt1 151
Swering, P. pt4 158
Szerlip, A. pt6 181

T

Takacs, A. S. pt6 111
Takeuchi, K. pt1 123
Talley, H. E. pt3 115
Templin, E. W. pt7 19
Thompson, B. W. pt4 48
Tinkham, R. J. pt7 12

Tischer, F. J. pt1 4
Tolles, W. E. pt5 231
Trumbo, D. E. pt4 3
Tuttle, W. N. pt2 23
Twersky, W. D. pt1 87

U

Ulstad, M. S. pt8 46

V

Vadasz, A. J. pt8 69
Van Valkenburg, M. E. pt2 3

W

Walcek, E. J. pt5 151
Walsh, J. E. pt1 243
Walter, C. M. pt4 8
Warren, C. S. pt4 62
Waters, W. D. pt1 13
Wassall, D. E. pt6 188
Waterman, A. T. pt1 184
Watt, C. W. pt6 135
Webster, R. R. pt7 57
Weekes, B. B. pt2 104

Weil, H. pt1 197
Wheeler, G. J. pt1 151
Wilds, R. B. pt1 48
Wileman, R. pt6 191
Wilke, W. E. pt5 86
Wilkins, W. B. pt6 141
Willett, H. M. pt4 8
Willrodt, M. pt5 77
Winkler, M. R. pt4 123
Winter, C. F. pt1 243
Wittmeyer, M. H. pt5 158
Worcester, K. pt6 104

Y

Yang, R. F. H. pt1 260
Yeh, L. P. pt1 104
Young, G. O. pt4 164
Young, H. A. pt9 11
Young, W. pt5 205

Z

Zadoff, S. A. pt4 173
Zarem, A. M. pt5 76
Zuk, P. pt3 122

INDEX TO SUBJECTS

Listings are by part number and page. Authors and paper titles may be determined from the tables of contents in the front part of this index.

A

Acceleration, High, Telemetry: pt5 20
Aerial Navigation Systems, Lightweight Kilowatt Klystron Amplifier for: pt3 100
Air Frame and Electronics Viewpoints, Project Management: pt9 23
Air Traffic Control, Digital Computer System for Terminal: pt5 61
Air Traffic Control Transponder, Compact RF Unit for: pt5 34
Airborne Equipment:
Data Acquisition Analysis and Appraisal of: pt5 3
Digital Tape Recording: pt5 168
Interference Generated by Devices Using Diode Rectifiers: pt5 25
Moving Target Radar, Reduced Platform Motion and Scanning Noise in: pt1 202
Transistor PDM System: pt5 13
Traveling-Wave Tube Applications: pt3 66
Alignment Techniques for Critical Band-Pass Circuitry: pt7 51
Amplifiers:

Compressor-Limiter Audio, for Studio: pt7 19
Distributed, and Virtual Delay Lines: pt2 62
Ferrite, Modified Semistatic: pt3 9
Klystron, Inherent Noise in: pt3 55
Klystron, Kilowatt, for Aerial Navigation Systems: pt3 100
Multistage 500-Megacycle: pt6 177
Operational Feedback in Data Processing: pt5 103
Parametric Electron Beam: pt3 13
Parametric, and Masers: pt3 3
Parametric, Using Lower-Frequency Pumping: pt3 23
"Squared" Input Stages for Low-Level Transistor: pt2 104
Stabilizing DC Transistor: pt2 94
Synthesis of Multichannel Amplifiers: pt2 99
Transistor, and Antenna Matching, Design Method for Coupling Applied to: pt2 47
Transistor, Diffused Silicon Logic: pt3 132
Transistor Feedback, Multiple Loop and Single Loop: pt2 78
Transistor Feedback, Root Locus Design of: pt2 87
Unilateral Solid-State Maser, Slow-Wave Structures for: pt3 29
Analog Computer, Anticipatory Display Design Through Use of: pt4 67
Analog Computer, Solving Microwave Problems by an: pt1 70
Analog Memory: pt4 108
Antennas:
Arrays, Impedance Properties of: pt1 175

Arrays, Logarithmically Periodic: pt1 161
Defocused Parabolic, Illuminating Curved Passive Reflector With: pt1 260
Low Gain Broad-Band: pt1 251
Matching, Design Method for Coupling Networks Applied to Transistor Amplifiers and: pt2 47
Parabolic Dome: pt1 272
Pattern Synthesis of the Most Truthful Approximation: pt1 178
Radar, Broad-Band, Low Sidelobe: pt1 243
Reflector-Type Periodic Broad-Band: pt1 266
Approach and Landing System: pt5 62

Arrays:
Antenna, Impedance Properties of: pt1 175
Arbitrarily Polarized: pt1 157
Concentric Loop: pt1 212
Logarithmically Periodic Antenna: pt1 161
Artificial Dielectrics, New Class of: pt1 21
Audio Amplifier, Compressor-Limiter, for Studio: pt7 19
Audio Oscillator, Transistor, Wide-Range Junction: pt2 74
Automatic Operation of Video Tape Equipment: pt7 43
Automatic Programming of AM and FM Broadcasting Stations: pt7 42
Automatic Radar Data Processing, Library of Blib Samples for Simulation of: pt4 8
Automatic Regulation of Breathing, Servomechanism for: pt5 224
Automatic Telemetry Meteorological Observation System: pt5 158
Avionics Systems, Project Direction in the Development of: pt9 13

B

Backward Wave Oscillator, Helix Type, With Extended Tuning Range: pt3 42
Beam Power Tube, Compact Kilowatt UHF: pt3 36
Binary Counter, An Emitter-Follower-Coupled, High-Speed: pt4 54
Bolometer Mounts, Broad-Band Waveguide: pt5 114
Breathing, Servomechanism for Automatic Regulation of: pt5 224
Broadcast Field, Frequency Measurements in: pt7 38
Broadcasting Stations, AM and FM, Automatic Programming of: pt7 42
Broadcasting Transmitters, AM, FM, and TV, Remote Control and Automatic Logging of: pt7 42

C

Cables, 500°C Low-Loss High-Frequency: pt6 121
Camera, Electronic Framing, for Millimicro-

second Photography: pt5 189
Camera Shutter, Millimicrosecond Kerr Cell: pt5 76
Capacitors, Ceramic, Monolithic Structure: pt6 45
Capacitors, Up-Grading Tantalytic: pt6 52
Capacitors, Voltage-Sensitive Semiconductor: pt3 72
Carbon Film Resistors, Deposited, Factors Affecting Formation of: pt6 71
Cascaded Actuators in Feedback Loop, Compensation for: pt4 182
Ceramic Capacitors, Monolithic Structure: pt6 45
Ceramic Components, Advances in: pt6 36
Ceramic Receiving Tubes, Stacked, Semi-automatic Production of: pt6 157
Chroma Key, Design and Use of: pt7 64
Circuits, RF, for Voltage-Tunable Magnetron: pt1 39
Circular Electric Waves in Circular Waveguide Containing Ferrite: pt1 123
Circulator, Hall Effect: pt3 83
Circulator, Tee: pt1 151
Coding, Picture, Computer Simulation Chain for Research on: pt4 41
Colleges, Engineering, Reliability and: pt6 10
Color Signal, NTSC, Head Drum Stabilization for Recording: pt7 29
Communication Systems, Radar Reflection Characteristics of the Moon and Earth-Moon-Earth: pt1 197
Communication Tool, Effective, Making the Mathematical Equation: pt9 41
Communications Systems, Economic Analysis in Long Term Planning of Military: pt8 3
Compass, Inertial, Earth's Rate Directional Reference: pt5 54
Compensation for Cascaded Actuators in Feedback Loop: pt4 182
Compensation of Multiloop Control Systems: pt4 177
Components, Ceramic, Advances in: pt6 36
Components, Sampling Versus Rating Dilemma on: pt6 81
Computers:
Analog, Anticipatory Display Through Use of: pt4 67
Analog, Solving Microwave Problems by an: pt1 70
Digital, System for Terminal Air Traffic Control: pt5 61
Diodes, Millimicrosecond Diffused Silicon: pt3 122
Distorted Filter Design With a Digital: pt2 10
Simulation Chain for Research on Picture Coding: pt4 41
Simulation, Digital, Experiments With Speech Using: pt7 3
Simulation of a Human Tracking Problem

on: pt4 286
 in Transistor Circuits, Mapping Vacuum
 Tube: pt4 47
 Contract, Government, Cost-Plus-Fixed-Fee:
 pt9 16
 Contract Implications of Military Electronics
 Reliability Requirements: pt6 32
 Control, Nonlinear Feedback, Systems, An-
 alysis of: pt4 233
 Control System, Numerical, for a Drivmatic
 Riveter: pt6 170
 Control Systems, Compensation of Multiloop:
 pt4 177
 Correlating Equipment for Medical Research,
 Electronic: pt5 206
 Counter, Binary, An Emitter-Follower-Cou-
 pled, High-Speed: pt4 54
 Counter, Transistorized Decade: pt6 181
 Crystal Filters, Modern Network Theory De-
 sign of Single-Sideband: pt2 33

D

Data Acquisition Analysis and Appraisal of
 Airborne Systems: pt5 3
 Data, Automatic Radar, Processing, Library
 of Blip Samples for Simulation of: pt4 8
 Data, Digital, Acquisition System for Instru-
 mentation Radars: pt5 41
 Data Link, GCA by Automatic Voice: pt4 28
 Data Preparation for Numerical Control of
 Machine Tools: pt4 3
 Data Processing Amplifiers, Operational Feed-
 back in: pt5 103
 Data Processing Equipment, Ground Based,
 Modular Packaging for: pt6 135
 DC Reference Voltage: pt6 104
 Decade Counter, Transistorized: pt6 181
 Demodulator, PAM/PDM, With Improved
 Synchronization: pt5 5
 Delay Lines, Virtual, and Distributed Ampli-
 fiers: pt2 62
 Delayed Pulse Generator as Variable Time
 Interval Standard: pt5 77
 Demodulator, S-Band Two-Phase: pt1 48
 Deposited Carbon Film Resistors, Factors Af-
 fecting Formation of: pt6 71
 Dielectric and Ferrite Loaded Waveguides,
 Field Displacement Effects in: pt1 135
 Dielectrics, Artificial, New Class of: pt1 21
 Diffused-Base Germanium Transistors: pt3 115
 Diffused Base Transistors, Switching Time Cal-
 culations for: pt3 141
 Diffused Silicon Computer Diodes, Millimicro-
 second: pt3 122
 Diffused Silicon Logic Amplifier Transistor: pt3
 132
 Digital Airborne Tape Recording: pt5 168
 Digital Computer, Predistorted Filter Design
 With a: pt2 10
 Digital Computer Simulation, Experiments
 With Speech Using: pt7 3
 Digital Computer, Terminal Air Traffic Con-
 trol System: pt5 61
 Digital Data Acquisition System for Instru-
 mentation Radars: pt5 41
 Digital Industrial Electronic Systems and
 Their Military Heritages: pt6 188
 Diodes:
 Millimicrosecond Diffused Silicon Com-
 puter: pt3 122
 Recovery Time Measurement in the Milli-
 microsecond Region: pt3 131
 Rectifiers, Interference Generated by Air-
 borne Devices Utilizing: pt5 25
 for Switching and Oscillator: pt3 176
 Display Design Through Use of Analog Com-
 puter, Anticipatory: pt4 67
 Distortion Reduction in TV Reception: pt7 65
 Distributed Amplifiers and Virtual Delay
 Lines: pt2 62
 Drone Tracking System with Lightweight Air-
 borne Package: pt5 151
 Duplexers During Their Time, Gas Tube, Con-
 trol of: pt3 105

E

Earth-Moon-Earth Communication Systems
 and Radar Reflection Characteristics of the
 Moon: pt1 197
 Earth's Rate Directional Reference Inertial
 Compass: pt5 54
 Economic Analysis in Long-Term Planning of
 Military Communications Systems: pt8 3
 Education, Industry's New Role in: pt9 7
 Electrical Power Problems in Fusion Research:
 pt5 126
 Electrocardiography, Electronic Aids to Ob-
 servations, Electrohystero-graphy and Fetal:
 pt5 216

Electrohystero-graphy and Fetal Electrocardi-
 ography: pt5 216
 Electromagnetic Waves, Forward Scatter by
 Spheres: pt1 86
 Electron Beam Amplifiers, Parametric: pt3 13
 Electron Tube, Compact Kilowatt UHF Beam:
 pt3 36
 Electron Tubes, Stacked Ceramic Receiving,
 Semiautomatic Production of: pt6 157
 Electron Tubes, Stacked, in Glass Envelopes:
 pt3 94
 Employee Losses, Minimizing, When R and D
 Operations Relocate: pt9 3
 Engineering Colleges, Reliability and: pt6 10
 Equation, an Effective Communication Tool:
 pt9 41

F

Feedback:
 Amplifiers, Transistor, Multiple Loop and
 Single Loop: pt2 78
 Amplifiers, Transistor, Root Locus Design
 of: pt2 87
 Control Systems, Nonlinear, Analysis of:
 pt4 233
 Loop, Compensation for Cascaded Actua-
 tors in: pt4 182
 Operational, in Data Processing Amplifi-
 ers: pt5 103
 Ferrite:
 Amplifier, Modified Semistatic: pt3 9
 Apertured Plates, Coincident Current Ap-
 plications of: pt4 62
 Circular Electric Waves in Circular Wave-
 guide Containing: pt1 123
 Line Width Measurement With a Cross-
 Guide Coupler: pt1 147
 Loaded Waveguides, Field Displacement
 Effects in: pt1 135
 Fetal Electrocardiography, Electrohystero-
 graphy and: pt5 216
 Fetal Heart Rate Measurements: pt5 231
 Field Displacement Effects in Dielectric and
 Ferrite Loaded Waveguides: pt1 135
 Filters:
 Mode Conversion: pt1 3
 Nonlinear, Random Function Probability
 Distributions After: pt4 164
 Predistorted, Design With a Digital Com-
 puter: pt2 10
 Single-Sideband Crystal, Modern Network
 Theory Design of: pt2 33
 Zobel, for Tchebycheff Insertion Loss, De-
 sign of Two-Section Symmetrical: pt2
 23
 Frequency Measurements in the Broadcast
 Field: pt7 38
 Frequency Measuring Using Paramagnetic
 Resonance in X Band: pt1 26
 Frequency Source, Transistorized Voltage Con-
 trollable: pt5 86
 Frequency Transformations, Graphical Inter-
 pretations for: pt2 42
 Function Generator, Transistorized All-Elec-
 tronic Cosine Sine: pt4 89
 Fusion Research, Electrical Power Problems in:
 pt5 126
 Fusion Research, Spectroscopy Aspects of: pt5
 139
 Fusion, Thermonuclear, Power Program, Ultra-
 high Vacuum Research in Support of: pt5
 140

G

Gas Tube Duplexers, Control During Their
 Relaxation Time: pt3 105
 Generator, Delayed Pulse, as Variable Time
 Interval Standard: pt5 77
 Generator, Transistorized All-Electronic Co-
 sine Sine Function: pt4 89
 Generators, Broad-Band Stabilized Micro-
 wave: pt5 98
 Glass Envelopes, Stacked Tubes in: pt3 94
 Graphical Interpretations for Frequency Trans-
 formations: pt2 42
 Ground-Controlled Approach by Automatic
 Voice Data Link: pt4 28

H

Hall Effect Circulator: pt3 83
 Heart, Fetal, Rate Measurements: pt5 231
 High Fidelity System, Home, Four-Track
 Stereotape Magazine for: pt7 12
 Human Dynamic Response, Tracking Research
 Applied to: pt4 254
 Human Tracking Problem on the UDEC III
 Computer, Simulation of a: pt4 286

I

Industrial Electronic Systems, Digital, and
 Their Military Heritages: pt6 188
 Industry's New Role in Education: pt9 7
 Inertial Compass, Earth's Rate Directional
 Reference: pt5 54
 Information Storage in Microspace: pt4 66
 Interference Generated by Airborne Devices
 Utilizing Diode Rectifiers: pt5 25

K

KDKA, Field Experience With Kahn Compati-
 ble Single-Sideband System Installed at: pt7
 28
 Kerr Cell Camera Shutter, Millimicrosecond:
 pt5 76
 Klystron Amplifier, Lightweight Kilowatt,
 for Aerial Navigation Systems: pt3 100
 Klystron Amplifiers, Inherent Noise in: pt3 55

L

Landing System and Approach: pt5 62
 Lenses, Luneberg, Theory and Design of: pt1
 219
 Library of Blip Samples for Simulation of Auto-
 matic Radar Data Processing: pt4 8
 Logic Amplifier Transistor, Diffused Silicon:
 pt3 132
 Luneberg Lenses, Theory and Design of: pt1
 219

M

Machine Tools, Data Preparation for Numeri-
 cal Control of: pt4 3
 Magnetron, Voltage-Tunable, RF Circuits for:
 pt1 39
 Man-Machine Control Systems, Optimization
 of: pt4 272
 Man-Machine Systems, Sibyl, A Laboratory
 for Simulation Studies of: pt4 277
 Man-Machine Systems, Synthesis of a Linear
 Quasi Transfer Function for the Operator in:
 pt4 263
 Maser Amplifiers, Unilateral Solid-State, Slow-
 Wave Structures for: pt3 29
 Maser Systems, Solid-State: pt3 28
 Masers and Parametric Amplifiers: pt3 3
 Mathematical Equation an Effective Com-
 munication Tool, Making the: pt9 41
 Medical Research, Electronic Correlating
 Equipment for: pt5 206
 Memory, Analog: pt4 108
 Metal-to-Ceramic Varistor, Thermally Fused:
 pt6 60
 Meteorological Observation System, Automatic
 Telemetering: pt5 158
 Microwave Generators, Broad-Band Stabil-
 ized: pt5 98
 Military Communications Systems, Economic
 Analysis in Long-Term Planning of: pt8 3
 Military Electronics Reliability Requirements,
 Contract Implications of: pt6 32
 Military Heritages, Digital Industrial Elec-
 tronic Systems and Their: pt6 188
 Millimicrosecond Diffused Silicon Computer
 Diodes: pt3 122
 Millimicrosecond Kerr Cell Camera Shutter:
 pt5 76
 Millimicrosecond Photography, Electronic
 Framing Camera for: pt5 189
 Millimicrosecond Region, Diode Recovery
 Time Measurement in: pt3 131
 Mode Conversion Filters: pt1 3
 Mode Conversion in Long Circular Waveguide,
 Effects of: pt1 13
 Modular Packaging for Ground Based Data
 Processing Equipment: pt6 135
 Monolithic Structure Concept for Ceramic
 Capacitors: pt6 45
 Moon-Earth Communication Systems and
 Radar Reflection Characteristics of the
 Moon: pt1 197
 Multiplexers, Waveguide and Strip Transmis-
 sion: pt1 54

N

Navigation Systems, Aerial, Lightweight Kilo-
 watt Klystron Amplifier for: pt3 100
 Networks:
 Coupling, Applied to Transistor Amplifiers
 and Antenna Matching: pt2 47
 Linear, Containing a Periodically Oper-
 ated Switch, Transmission Through a:
 pt2 34
 Nonreciprocal TEM-Transmission-Line:
 pt1 131
 Optimum Synthesis of RC Ladder: pt2 46
 Single-Sideband Crystal Filter Design:
 pt2 33

Solution of the Right Triangle Problem: pt4 123

Neutron Damage in Germanium and Silicon Transistors, Comparison of: pt3 148
Noise, Additive Stationary, Prediction of Derivatives of Polynomial Signals in: pt4 131
Noise, Inherent, in Klystron Amplifiers: pt3 55
Noise in Sampled-Data Systems, Statistical Invariance of: pt4 173
Nonlinear Feedback Control Systems, Analysis of: pt4 233
Nonreciprocal TEM-Transmission-Line Network: pt1 131
Numerical Control of Machine Tools, Data Preparation for: pt4 3
Numerical Control System for a Drivmatic Riveter: pt6 170

O

Obstacle Gain at Microwave Frequencies: pt1 231
Obstetrics, Electronic Aids to: pt5 216
Operational Feedback in Data Processing Amplifiers: pt5 103
Optimization of Man-Machine Control Systems: pt4 272
Optimum Linear Estimation for Random Processes: pt4 158
Organic Coatings for the Protection of Printed Circuits: pt6 169
Oscillator, Helix Type Backward Wave, With Extended Tuning Range: pt3 42
Oscillator and Switching, New Diode for: pt3 176
Oscillator, Wide-Range Junction Transistor Audio: pt2 74

P

Parabolic Defocused Antenna, Illuminating Curved Passive Reflector With: pt1 260
Parabolic Dome Antenna: pt1 272
Paramagnetic Resonance in X Band, Frequency Measuring Using: pt1 26
Parametric Amplifiers and Masers: pt3 3
Parametric Amplifiers Using Lower-Frequency Pumping: pt3 23
Parametric Electron Beam Amplifiers: pt3 13
Photography, Millimicrosecond, Electronic Framing Camera for: pt5 189
Piano, Research and Development on: pt7 27
Picture Coding, Computer Simulation Chain for Research on: pt4 41
Polynomial Signals in Additive Stationary Noise, Prediction of Derivatives of: pt4 131
Power Handling Capacity of Slab Lines: pt1 35
Power Supplies, Static-Magnetic Regulated DC: pt6 87
Power Supply Design, Regulated, Thermal Considerations in: pt6 191
Prediction of Derivatives of Polynomial Signals in Additive Stationary Noise: pt4 131
Predictive Quantizing of Television Signals: pt4 147
Printed Circuits, Insulated Flexible: pt6 141
Printed Circuits, Organic Coating for the Protection of: pt6 169
Printed Wiring, Honeycomb Structure Rigidizes, for High Vibration: pt6 166
Probability Distributions, Random Function, After a Nonlinear Filter: pt4 164
Production, Semiautomatic, of Stacked Ceramic Receiving Tubes: pt6 157
Programming, Automatic, of AM and FM Broadcasting Stations: pt7 42
Project Direction in the Development of Avionics Systems: pt9 13
Project Management, Air Frame and Electronics Viewpoints: pt9 23
Project Organization, Publication and: pt9 26
Publications and the Project Organization: pt9 26
Pulse Amplitude Modulation, PAM/PDM Demodulator With Improved Synchronization: pt5 5
Pulse Code Modulation, Compatible PCM/FM System: pt5 4
Pulse, Delayed, Generator as Variable Time Interval Standard: pt5 77
Pulse Duration Modulation System, Transistor Airborne: pt4 13
Pulse Packing Densities and Transfer Rates, Achieving Maximum: pt4 48

Q

Quantizing of Television Signals: pt4 147

R

Radar:

Antenna, Broad-Band Low Sidelobe: pt1 243
Data Processing, Automatic, Library of Bib Samples for Simulation of: pt4 8
Instrumentation, Digital Data Acquisition System for: pt5 41
Moving-Target, Airborne, Reduced Platform Motion and Scanning Noise in: pt1 202
Reflection Characteristics of the Moon and Earth-Moon-Earth Communication Systems: pt1 197
Random Function Probability Distributions After a Nonlinear Filter: pt4 164
Random Processes, Optimum Linear Estimation for: pt4 158
Rating Versus Sampling Dilemma on Components: pt6 81
Receiver Circuitry, Critical Band-Pass, Alignment Techniques for: pt7 51
Receiver, Transistorized Television: pt7 57
Receiving Tubes, Stacked Ceramic, Semiautomatic Production of: pt6 157
Recording, Digital Airborne Tape: pt5 168
Recording the NTSC Color Signal, Head Drum Stabilization for: pt7 29
Rectifier, A Medium Power Silicon Controlled: pt3 166
Rectifiers, Diode, Interference Generated by Airborne Devices Utilizing: pt5 25
Redundancy Approach, the Group for Optimum Design for Reliability: pt6 23
Reflector with Defocused Parabolic Antenna, Illuminating Curved Passive: pt1 260
Reflector-Type Periodic Broad-Band Antennas: pt1 266
Reliability:
Considerations, Integrating, Into Systems Analysis: pt6 30
Contract Implications of Military Requirements: pt6 32
and Engineering Colleges: pt6 10
Optimum Design for, through the Group Redundancy Approach: pt6 23
Tests, Confidence That Can Be Placed on: pt6 14
of Weapon Systems During Flight-Readiness Checkout: pt6 3
Remote Control and Automatic Logging of AM, FM, and TV Broadcasting Transmitters: pt7 42
Report Writing, Two-Hour Course in: pt9 30
Research and Development Operations Relocate, Minimizing Employee Losses When: pt9 3
Resistors, Deposited Carbon Film, Factors Affecting Formation of: pt6 71
Right Triangle Problem, Network Solution of the: pt4 123
Riveter, Drivmatic, Numerical Control System for: pt6 170
Root Locus Design of Transistor Feedback Amplifiers: pt2 87

S

Sales Engineer, Human Catalyst of the Electronics Industry: pt9 11
Sampled-Data Systems, Statistical Invariance of Noise in: pt4 173
Sampled Data Theory, Simplifying Additions to: pt4 197
Sampling Versus Rating Dilemma on Components: pt6 81
Scanning, Rapid-, Phased Array for Wave Propagation Measurements: pt1 184
Scatter, Forward, of Electromagnetic Waves by Spheres: pt1 86
Scatter, Tropospheric, Propagation Data, Statistical Study of: pt1 104
Semiconductor Capacitors, Voltage-Sensitive: pt3 72
Servomechanism for Automatic Regulation of Breathing: pt5 224
Servos, Digital-Hydraulic: pt4 239
Sibyl, A Laboratory for Simulation Studies of Man-Machine Systems: pt4 277
Simulation:
of Automatic Radar Data Processing, Library of Bib Samples for: pt4 8
of Human Tracking Problem on the UDEC III Computer: pt4 286
of Man-Machine Systems, Sibyl, A Laboratory for: pt4 277
Speech Experiments Using Digital Computer: pt7 3
Single-Sideband Crystal Filters, Modern Network Theory Design of: pt2 33

Single-Sideband System Installed at KDKA, Kahn Compatible, Field Experience With: pt7 28
Slides, Should They Be Used in a Technical Presentation: pt9 35
Solid-State Maser Amplifiers, Unilateral, Slow-Wave Structures for: pt3 29
Solid-State Maser Systems: pt3 28
Space:
and High Vacuum: pt5 147
Human Capability in: pt5 202
Manned Operations, Dynamic Survival Potential in: pt5 196
Survival and Performance of Man in: pt5 198
Travel, Future Instrumentation Problems in: pt5 205
Travel, Measurements, State of Art in: pt5 205
Spectroscopy Aspects of Fusion Research: pt5 139
Speech Bandwidth Compression Techniques: pt7 11
Speech Kit, Multiaudience, Multipurpose: pt9 50
Speech Using Digital Computer Simulation, Experiments With: pt7 3
Standard, Variable Time Interval, Delayed Pulse Generator as: pt5 77
Statistical Invariance of Noise in Sampled-Data Systems: pt4 173
Statistical Study of Tropospheric Scatter Propagation Data: pt1 104
Stereotape Magazine, Four-Track, for Home Hi-Fi: pt7 12
Storage, Information, in Microspace: pt4 66
Strip Transmission Line and Waveguide Multiplexers: pt1 54
Studio, Compressor-Limiter Audio Amplifier for: pt7 19
Surface Waves on Right-Angled Wedge: pt1 101
Switch, Transmission Through a Linear Network Containing a Periodically Operated: pt2 34
Switches, $P\pi N$: pt3 172
Switching and Oscillator, New Diode for: pt3 176
Switching Time Calculations for Diffused Base Transistors: pt3 141
Synthesis of Linear Quasi Transfer for the Operator in Man-Machine Systems: pt4 263
Synthesis of Multichannel Amplifiers: pt2 69
Synthesis, Topological: pt2 3
Systems Analysis, Integrating Reliability Considerations Into: pt6 30

T

Tantalum Capacitors, Up-Grading: pt6 52
Tape Equipment, Video, Automatic Operation of: pt7 43
Tape Recording, Digital Airborne: pt5 168
Tchebycheff Insertion Loss, Design of Two-Section Symmetrical Zobel Filters for: pt2 23
Tee Circulator: pt1 151
Telemetering Meteorological Observation System, Automatic: pt5 158
Telemetry, High Acceleration: pt5 20
Television Receiver, Transistorized: pt7 57
Television Reception, Distortion Reduction in: pt7 65
Television Signals, Predictive Quantizing of: pt4 147
Temperature Coefficient Measurement, Dynamic: pt6 111
Thermal Considerations in Regulated Power Supply Design: pt6 191
Thermally Fused Metal-to-Ceramic Vamistor: pt6 60
Thermonuclear Fusion Power Program, Ultra-high Vacuum Research in Support of the: pt5 140
Timing Systems, Heterogeneous or Homogeneous: pt8 14
Topological Synthesis: pt2 3
Tracking Problem, Human, Simulation on UDEC III Computer: pt4 286
Tracking Research Applied to Hyman Dynamic Response: pt4 254
Tracking Systems, Drone, With Lightweight Airborne Package: pt5 151
Transfer Function for the Operator in Man-Machine Systems, Synthesis of: pt4 263
Transfer Function, Quasi, for the Operator in Man-Machine Systems, Synthesis of: pt4 263
Transfer Rates, Achieving Maximum Pulse Packing Densities and: pt4 48

Transistors:

Airborne PDM System: pt5 13
 Amplifiers and Antenna Matching, Coupling Networks Applied to: pt2 47
 Amplifiers, "Squared" Input Stages for Low-Level: pt2 104
 Amplifiers, Stabilizing DC: pt2 94
 Audio Oscillator, Wide-Range Junction: pt2 74
 Circuits, Mapping Vacuum Tube Computers in: pt4 47
 Diffused-Base Germanium: pt3 115
 Diffused Base, Switching Time Calculations for: pt3 141
 Diffused Silicon Logic Amplifier: pt3 132
 Feedback Amplifiers, Multiple Loop and Single Loop: pt2 78
 Feedback Amplifiers, Root Locus Design of: pt2 87
 Germanium and Silicon, Comparison of Neutron Damage in: pt3 148
 High Power Silicon: pt3 157
 Transistorized Equipment:
 Cosine Sine Function Generator: pt4 89
 Decade Counter: pt6 181
 Television Receiver: pt7 57
 Voltage Controllable Frequency Source: pt5 86
 Transmission Line Network, Nonreciprocal TEM: pt1 131

Transmission Line, Strip, and Waveguide Multiplexers: pt1 54
 Transmission Lines, Slab, Power Handling Capacity of: pt1 35
 Transmission Through a Linear Network Containing a Periodically Operated Switch: pt2 34
 Transmitters, AM, FM, and TV Broadcasting, Remote Control and Automatic Logging of: pt7 42
 Transponder, Air Traffic Control, Compact RF Unit for: pt5 34
 Traveling-Wave Tube, Crossed-Field, the M-J Tube: pt3 60
 Triangle Problem, Network Solution of the Right: pt4 123
 Tropospheric Scatter Propagation Data, Statistical Study of: pt1 104

V

Vacuum, High, and Space: pt5 147
 Vacuum, Ultrahigh, Research in Support of the Thermonuclear Fusion Power Program: pt5 140
 Vamistor, Thermally Fused Metal-to-Ceramic: pt6 60
 Vibration, Honeycomb Structure Rigidizes Printed Wiring for: pt6 166
 Video Tape Equipment, Automatic Operation of: pt7 43

Voice Data Link, GCA by Automatic: pt4 28
 Voltage, DC, Reference: pt6 104
 Voltage-Sensitive Semiconductor Capacitance: pt3 72
 Voltage-Tunable Magnetron, RF Circuits for: pt1 39

W

Wave Propagation Through Random Distributions of Spheres: pt1 87
 Waveguides:
 Bolometer Mounts: pt5 114
 Circular, Containing Ferrite, Circular Electric Waves in: pt1 123
 Circular, Mode Conversion in: pt1 13
 Field Displacement Effects in Dielectric and Ferrite Loaded: pt1 135
 H-Guide, at Microwaves and Millimeter Waves: pt1 4
 Multiplexers, Strip Transmission Line and: pt1 54
 Weapon Systems During Flight-Readiness Checkout, Upgrading the Reliability of: pt6 3
 Writing, Report, Two-Hour Course in: pt9 30

Z

Zobel Filters for Tchebycheff Insertion Loss, Design of Two-Section Symmetrical: pt2 23

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Professional Group on Broadcast and Television Receivers

The field of broadcast receivers is one which is closely associated with the general public, perhaps more so than any other branch of the radio engineering field. In fact, to the layman the term "radio" is synonymous with "broadcast receiver."

As a result, the receiver engineer has been concerned with an additional factor not generally common to other fields, namely, that of responding to—or endeavoring to create—public demand for a product. This factor has played a prominent role in such developments as FM, car radios, portable receivers, and black-and-white television sets. It is now conspicuously evident in connection with current efforts to produce and market color television receivers.

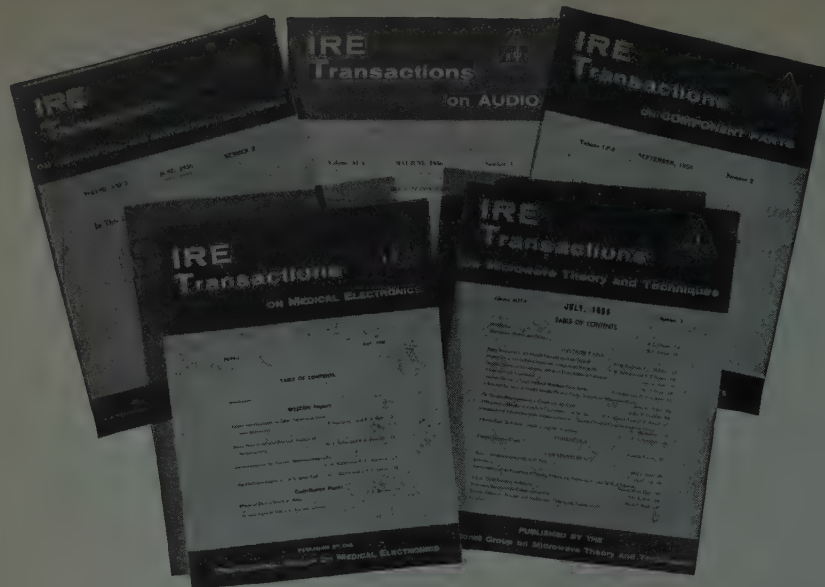
The IRE Professional Group on Broadcast and Television Receivers is playing a major role in making available vitally needed technical information, not only on color television, but on all aspects of the receiver field. Through this exchange of information, the radio and television industry is gaining important data which will be helpful in solving the engineering problems it faces and in successfully meeting the "public demand" factor mentioned above.

The Group has been particularly active in sponsoring technical sessions at most of the national meetings held throughout the country during the year: the Radio Fall Meeting, the Spring Television Conference in Cincinnati, and the IRE National Convention, and Wescon to mention but a few.

The Group also publishes its own technical publication, called *Transactions*, which is distributed to some 1900 members as a part of their \$2.00 assessment fee. The *Transactions*, which is published on a quarterly basis, has become a chief source of information on the latest technical developments in the field of broadcast and television receivers.

W. R. G. Baker

Chairman, Professional Groups Committee



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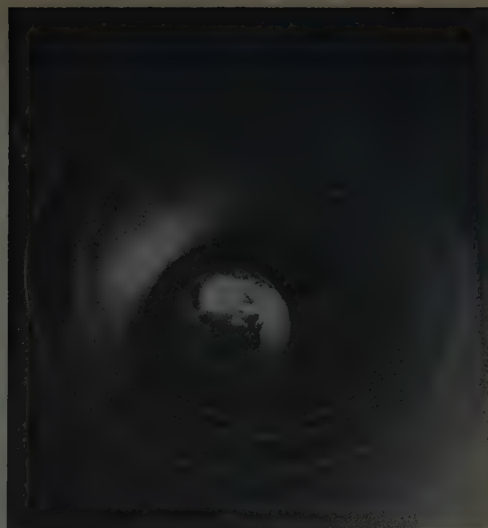
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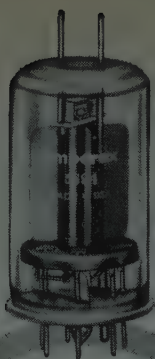
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DC Grid No. 1 Voltage	-80	-80	-80 volts
DC Plate Current	2x80	2x100	2x90 ma
DC Grid No. 2 Current	17	16	14 ma
DC Grid No. 1 Current (approx.)	2x1.5	2x2.5	2x1.7 ma
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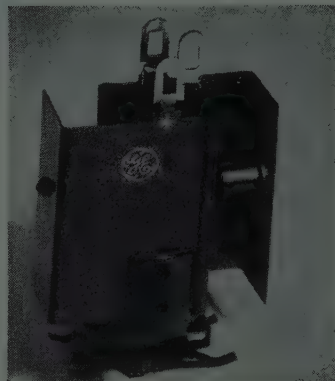


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(Continued from page 98A)

Germanium Rectifiers

The General Electric Co., Syracuse, N. Y., has revised its line of snap-in germanium rectifiers for the direct replacement of selenium rectifiers in television sets.



Now, one 400-milliamperere halfwave and one 400-milliamperere doubler rectifier replace the entire line of five replacement types.

In addition the prices of these rectifiers have been reduced so that they now sell for 10 and 5 per cent less respectively than the lowest rated germanium TV replacement rectifiers previously in the line.

Germanium TV rectifiers do not "age," wear out or burn up when used within their ratings. Thus their life expectancy is characterized by engineers as "unlimited."

The two devices have been JETEC type designated 1N1008 for the halfwave type and 1N1016 for the doubler type.

Both devices deliver 400-milliamperere dc output current into a load at 70°C or 158°F. Both devices are rated at a peak inverse voltage of 380 volts and an RMS input voltage of 130 volts. Neither device need be derated since there is a complete absence of aging characteristics.

**Glass-To-Metal
Sealing Alloys**

Wilbur B. Driver Co., 1875 McCarter Hwy., Newark 4, N. J., has recently printed a new two color four page brochure describing Rodar*, Niron 46, and Niron 52 alloys for glass-to-metal hermetic sealing. Complete details on each of these tailor made alloys, including nominal analysis, average mechanical properties, and average physical constants are given. A thermal expansion chart showing expansion in mills per inch by °F is also shown. The firm supplies resistance, chemical and mechanical alloys in wire, rod, ribbon, strip and foil.

* T.M. International Nickel Co.

**Variable Frequency
Oscillators**

Variable crystal controlled oscillators combining small size and high repeatability are now available from the Electronics Division, Bulova Watch Co., P-1102, 40-06 62 St., Woodside 77, N. Y.



Designated the VCF Series, the oscillators feature automatic frequency control or variation of nominal frequency by the application of an external voltage.

Frequency range is from 10 kc to 20 mc, with obtainable variations up to 6 cps at 10 kc, and up to 12 kc at 20 mc. The resolution on these shifts is infinite depending on the stability and resolution of the modulating voltage. Drift, after stabilization, can be kept to less than 1 part in 1 million.

The transistorized or tube type variable oscillators find numerous applications, such as automatic frequency controls for missile guidance systems, automatic frequency controls for laboratory aircraft and missile frequency standards, closed loop frequency systems, transducer-actuated measuring devices, and many others.

They are available in Bulova Types AM-03, AM-02, AM-015, MB 101-V and OS-1. While temperature controlled ovens are normally incorporated in the VCF Series, they are also available without ovens.

**Secondary Pressure
Standard**



A new portable secondary standard Type Z3401 for calibration and direct parameter measurement is now available from Wiancko Engineering Co., 255 No. Halstead Ave., Pasadena, Calif. Interchangeable plug-in units, accommodating gage, differential, and absolute pressures,

(Continued on page 106A)

TUNG-SOL POWER TRANSISTORS IMPROVED THREE WAYS BY:

NEW

Cold-Weld



SEAL

Tung-Sol's new true cold-weld seal represents a major advance in transistor technology. An exclusive Tung-Sol development, cold-weld sealing increases TO-3 outline package efficiency and brings designers a threefold bonus in over-all transistor performance.

Improved thermal qualities. The cold-weld process produces a hermetic, copper-to-copper seal and makes possible a 100% copper transistor with thermal properties superior to previous high power types.

Improved reliability. Cold-weld encapsulation eliminates heat damage, "splash", and heat-caused moisture that can impair transistor performance.

Longer efficient life. Even through temperature fluctuations that cause "breathing", the cold-weld seal stays vacuum-tight, moisture-proof—result of actual integration of the copper molecules during sealing.

Tung-Sol power switches with the new cold-weld seal withstand the most rigid combination of tests given any transistor—the 100 psi "bomb" immersion test and the critically sensitive Mass Spectrometer leak test. Further, they meet all military environmental requirements. For full data on the improved Tung-Sol types . . . to fill any transistor need, contact: Semiconductor Division, Tung-Sol Electric Inc., Newark 4, New Jersey.

THESE TUNG-SOL HIGH POWER (TO-3 OUTLINE) TRANSISTORS FEATURE THE NEW, COLD-WELD SEAL

Type	BVCES (VBE = +1.0v) Volts (Min)	BVCEO (IB = 0) Volts (Min)	hFE (IC = 1.0 A)	hFE (IC = 2.0 A)
2N378	—40	—20	50	30
2N379	—80	—40	50	30
2N380	—60	—30	70	50
2N459	—105	—60	50	30



TO-3

IMPROVED SPECIFICATIONS OF TUNG-SOL COLD-WELDED HIGH POWER TRANSISTORS.

Collector Dissipation @ 25°C*...50 Watts
Collector Dissipation @ 55°C*...25 Watts
Thermal Resistance.....1.2° C/Watt Max.
ICBO @ VCB = —25v T = 25°C...0.5 Ma Max.
ICBO @ VCB = —25v T = 85°C...7.5 Ma Max.
Storage Temperature.....—55 to +100°C

*Mounting base temperature

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- ★ Thermocouple Wires — Precious metal.
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These manufacturers have invited PROCEEDINGS readers to write for literature and further technical information. Please mention your IRE affiliation.

(Continued from page 104A)

provide an overall accuracy of 0.05 per cent for ranges up to 2500 psig, psid, or psia. Plug-in units for measuring forces, accelerations, and temperatures will soon be available. The standard can be rack mounted. Used with a remote pickup, it provides a single-channel FM system, since it incorporates a precision FM oscillator and an integral power supply. Two standards used together provide a versatile digital ratio measuring system, requiring in addition only a Wiancko dual heterodyne unit and a ratio counter.

Two-Channel Medical Scope

For monitoring and comparison of two physiological signals, engineered specifically for medicine, the new Duo-Trace Cardioscope developed by Levinthal Electronic Products, Inc., 979 Stanford Industrial Park, Palo Alto, Calif. simultaneously displays two independent physiological signals.



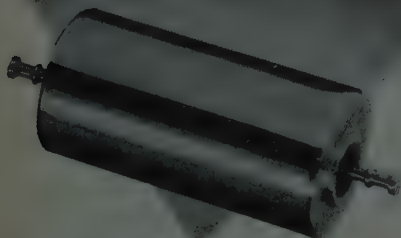
A typical application of the new instrument is simultaneous observation of electrocardiograph and electroencephalograph signals for monitoring anoxia in surgery. However, other applications include recovery-room and cardiac-ward monitoring, cardiac catheterization, and phonocardiography.

Displaying two traces on a 5-inch, long-persistent screen, the new instrument has a frequency range to 2,000 cps; a continuously variable sweep rate from 7.5 to 100 mm per second; a sensitivity of 330 microvolts per centimeter. An optional accessory preamplifier increases the sensitivity to 10 microvolts per centimeter. Baseline stability circuits restore the trace to the center of the screen approximately one second after it has been driven off scale by an excessive artifact.

The new instrument weighs 35 pounds. It operates from standard 115 v 50/60 cps current. Other input voltages for export

(Continued on page 108A)

New **LOW LOSS** Solid Ultrasonic Delay Lines by **BLILEY**



This new series of solid ultrasonic delay lines, in range 2 to 50 microseconds, employs special barium titanate transducers to reduce loss level. Loss levels, into 100 ohm terminations, range from 6 to 10 db compared to 35 db for conventional types.

TYPICAL CHARACTERISTICS OF A 2 USEC. BLILEY LOW LOSS LINE:

- Delay time: 2 usec.
- Type: double ended absorber
- Center frequency: 30 mc.
- Termination: 500 ohms.
- Capacity: 385 mmf.
- Insertion loss to first reflected pulse: 5 db.
- Third time signal: down 30 db.
- Delay time variation from —20 to +60°C.: ±.01 usec.

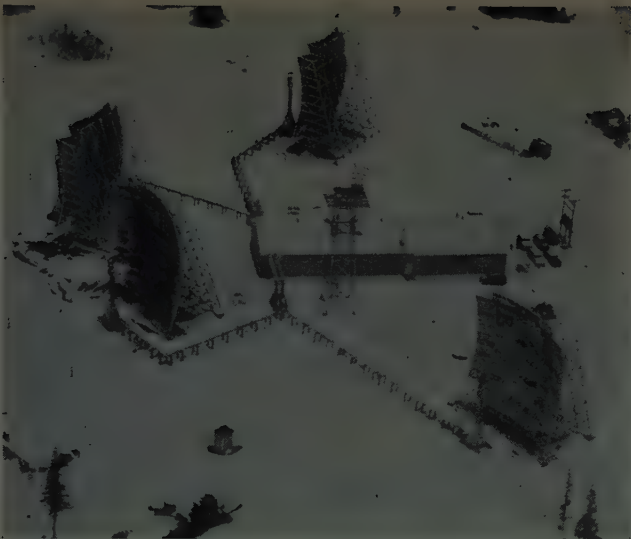
Request Bulletin #S13 for details.

Bliley

BLILEY ELECTRIC COMPANY

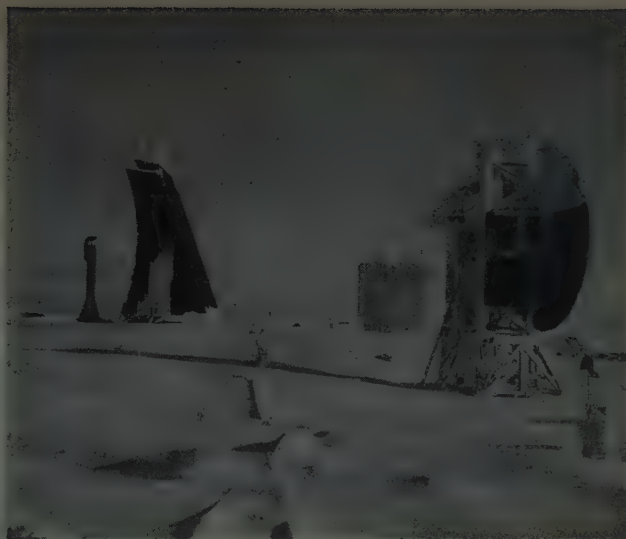
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WHITE ALICE

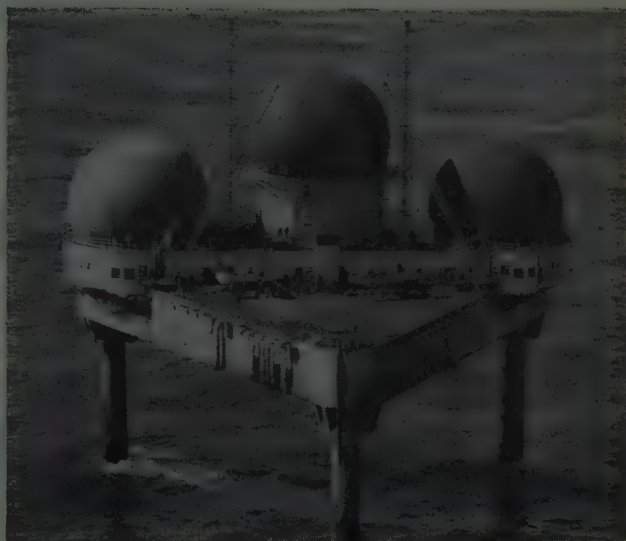
WESTERN ELECTRIC PHOTO



DEW LINE



POLE VAULT



TEXAS TOWERS

EIMAC KLYSTRONS performance proved in original Tropo-Scatter systems

Eimac klystrons are used in nearly every major military and commercial tropo-scatter system in the world. The list is impressive: Pole Vault, Texas Towers, Dew Line, White Alice, SAGE, NATO, Florida-Cuba TV, and numerous commercial networks. They have been selected for systems from Norway to North Africa, from the Arctic Circle to the Andes, from the United States to the Far East.

In most of these systems Eimac klystrons are used exclusively. The reason is simple: Eimac-pioneered external-cavity klystrons make it possible to generate high power at ultra-high frequencies simply, reliably and at low cost. With the Eimac external-cavity system, tuning cavities, couplers and magnetic circuitry are all external to and separate from the tube. This permits ex-

ceptionally wide tuning range and simplifies equipment design. Cost is lowered because this external circuitry is a permanent part of the transmitter and is not repurchased when tubes are replaced.

The reliability of these high-performance devices is exceptional. Some of the original Eimac klystrons installed in Project Pole Vault—the first major tropo-scatter network ever established—are still going strong with more than 25,000 hours of air time logged to their credit.

Eimac manufactures a complete line of amplifier and pulse klystrons covering the most important areas of the UHF spectrum. Write our Application Engineering Department for specific information.

EITEL-McCULLOUGH, INC.

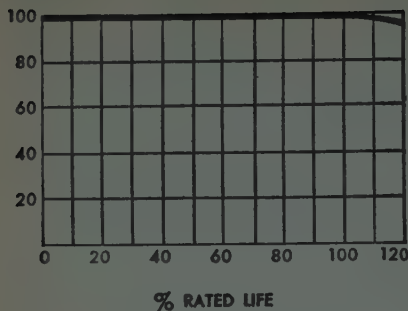
SAN CARLOS, CALIFORNIA

Eimac First with ceramic tubes that can take it



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EIMAC
San Carlos

% STILL
OPERATING



If you want reliable transformers

...don't overlook this old solution

Right now, you demand more from transformers than ever before. You must have high reliability, even at extreme altitudes, and you need smaller lighter units.

Used, and *proved*, for decades, oil-encased transformers should not be forgotten in a search for new methods.

Everyone knows the advantages: effective convection of heat, excellent insulating properties, complete insurance against hidden leaks. Oil-sealed types (with a nitrogen bubble) are good, light, high-altitude transformers. Gas-free oil-filled types (with a bellows to allow for heat expansion) withstand very high voltage stresses. Except in the smallest sizes, they save space, too.

You can place several high voltage units close together in a single oil-filled case, and save case weight. Those connections moved inside the case no longer need large insulators. Even the units themselves can be smaller. This all adds up—particularly in high altitude service—to interesting savings in space and weight.

We make all sorts of transformers and special assemblies for the communication industry: encapsulated, cast in epoxy or foam, and just potted in pitch. But oil transformers still have an important place.

Whatever type you need, we'll be glad to hear from you. Our facilities in design, production, and quality control are at your service. Our experience, too.

CALEDONIA
ELECTRONICS AND TRANSFORMER CORPORATION

Dept. PI-12, Caledonia, N. Y.

In Canada: Hackbusch Electronics, Ltd.
23 Primrose Ave., Toronto 4, Ontario



NEWS New Products



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(Continued from page 106A)

are available on special order. In surgery, the Duo-Trace Cardioscope is ordinarily located on an optional 5 foot high stainless steel cart with conductive casters to meet operating room requirements.

For permanent recording of signals, scope provides an output jack for each

channel to which standard ECG or other recording equipment may be attached.

Motor Tach Generator

A new Size 8 Servo Motor Tachometer Generator with an operating temperature range of -55° to $+125^{\circ}\text{C}$ has been developed by John Oster Manufacturing Co., Avionic Div., 1 Main St., Racine, Wis. Type 8MTG-6202 series meets the environmental requirements of MIL-E-5272A, has a rotor moment of inertia of 1.15 gm. cm^2 , weighs 3.1 ounces and is housed in a passivated stainless steel case. The 2 phase motor has 26 volts excitation

(Continued on page 110A)

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—SPECIFY—

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LOW-LOSS RF LACQUER

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Trademark

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IDEAL COIL
IMPREGNANT

- Q-Max, an extremely low loss dielectric impregnating and coating composition, is formulated specifically for application to VHF and UHF components. It penetrates deeply, seals out moisture, provides a surface finish, imparts rigidity and promotes stability of the electrical constants of high frequency circuits. Its effect upon the "Q" of RF windings is practically negligible.
- Q-Max applies easily by dipping or brushing, dries quickly, adheres well, meets most temperature requirements. Q-Max is industry's standard RF lacquer. Engineers who know specify Q-Max! Write for new illustrated catalog.

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MARLBORO, NEW JERSEY—Telephone: Freehold 8 1880

Pacific Coast Branch: 120 SANTA BARBARA ST., SANTA BARBARA, CAL.—Woodland 2-1712-4



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★ improved
★ faster
★ completely
automatic

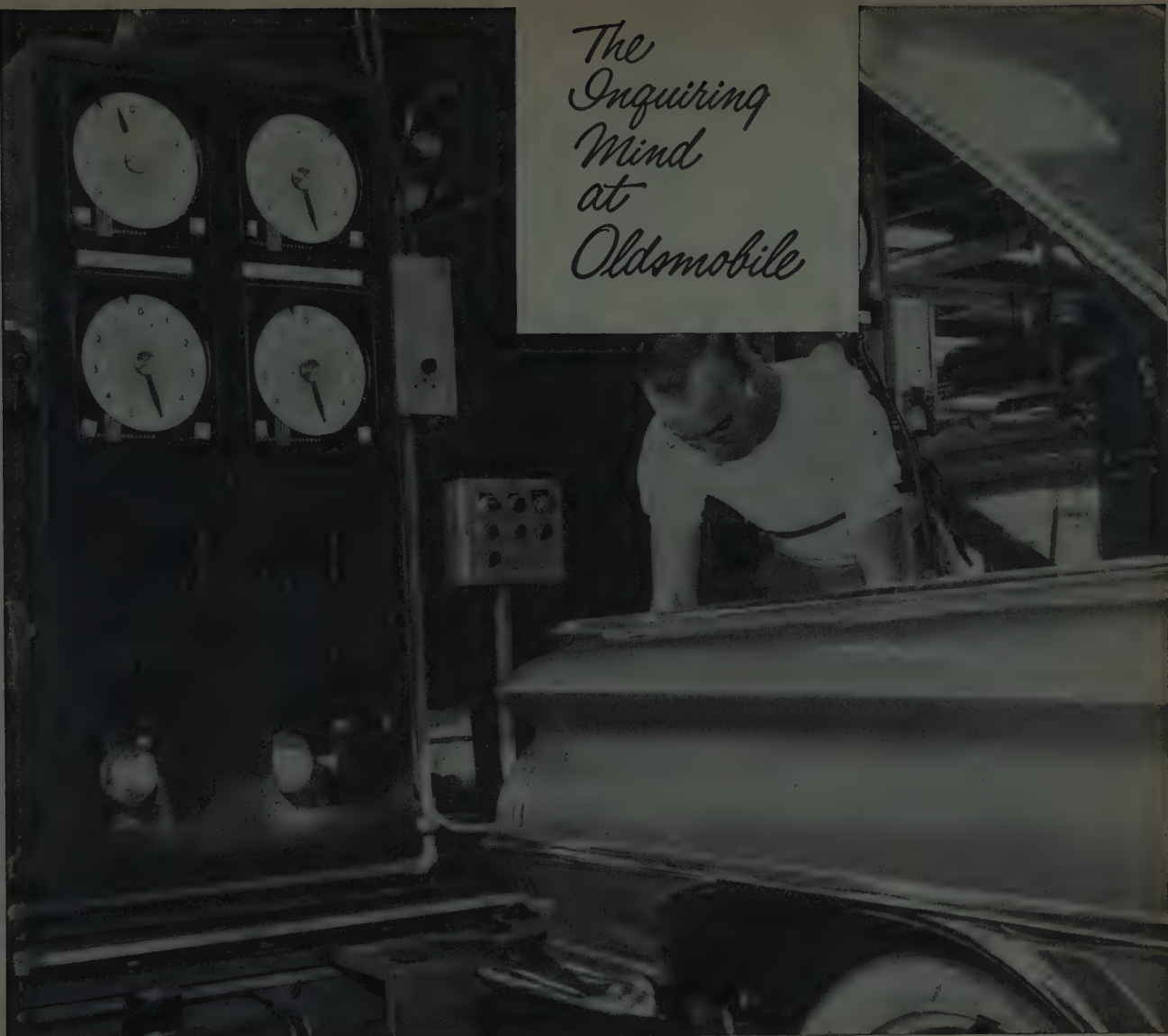
BW2 BOBBIN winder

rugged, versatile, high speed winder for
bobbins, solenoids, resistors, relays and
other random-wound coils.



Boesch Manufacturing Co., Inc. Danbury, Conn.

*The
Inquiring
Mind
at
Oldsmobile*



no.5
OF A SERIES

LIGHTING YOUR WAY TO A SAFER FUTURE

Safeguarding lives is the aim of Oldsmobile's new electronic headlamp aiming device that makes sure every Oldsmobile has perfect "see-ability".

Night driving safety depends upon how precisely headlamps are aimed. Minute errors in adjustment can mean the difference of several square feet in light area on the road. To be completely on the "safe side", Oldsmobile aiming standards specify that lights be aimed *twice* as accurately as required by state laws.

To make certain that every light is aimed perfectly, Oldsmobile engineers developed an ingenious electronic device that effectively measures light intensity and direction, even at Oldsmobile's highest production rate.

On the assembly line, every car is automatically shuttled to the aiming platform where two probes rise out of the floor and "feel" the exact location of the car. The "eyes"

of the aiming device then align themselves with the centerline of the car. A series of photoelectric cells instantly record the light intensity and direction on large dials. A built-in scanning circuit then inspects all settings of the headlamps to make certain they are accurate. If there is an error, a colored soap solution is automatically sprayed on the windshield, and the headlamps are re-aimed.

Oldsmobile takes pride in producing an automobile as advanced in every respect as modern technology can make it. However, you owe it to yourself to have your headlamps periodically checked. As part of General Motors' public-spirited "Aim to Live" program, your Oldsmobile Dealer is featuring headlamp aiming, as well as other important safety services for you. Stop in soon . . . and while you are there, take a test drive in a new Olds—sales leader of the medium price class.

OLDSMOBILE DIVISION, GENERAL MOTORS CORP.

OLDSMOBILE ➤

**Pioneer In Progressive Engineering
...Famous for Quality Manufacturing**

Tarzian

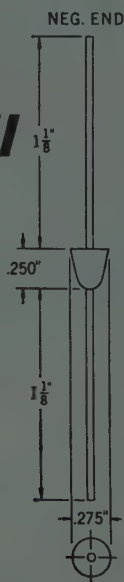
F Series Silicon Rectifiers...

UTMOST

... in Performance

S.T. Type	Max. Peak Inverse Volts	Max. RMS Volts	Current Ratings—Amperes											
			Max. D.C. Load			Max. RMS			Max. Recurrent Peak			Surge 4MS Max.		
			55°C	100°C	150°C	55°C	100°C	150°C	55°C	100°C	150°C	55°C	100°C	150°C
F-2	200	140	.75	.5	.25	1.875	1.25	.625	7.5	5.	2.5	75	75	35
F-4	400	280	.75	.5	.25	1.875	1.25	.625	7.5	5.	2.5	75	75	35
F-6	600	420	.75	.5	.25	1.875	1.25	.625	7.5	5.	2.5	75	75	35

... in Ultra Small Size



... in Low Price

Tarzian

research, engineering and production know-how have combined to develop the utmost in a small size, very low cost silicon rectifier with giant performance. If your problem is miniaturization, or cost, or tough application, the solution is in the Tarzian F series.

Send for Design Note #31

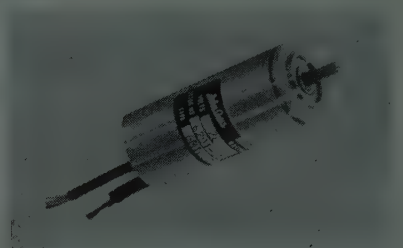
Sarkes Tarzian, Inc., Rectifier Division
DEPT. P-4, 415 NORTH COLLEGE AVE., BLOOMINGTON, INDIANA

IN CANADA: 700 WESTON RD., TORONTO 9, TEL. ROGER 2-7535 EXPORT: AD AURIEMA, INC., NEW YORK CITY



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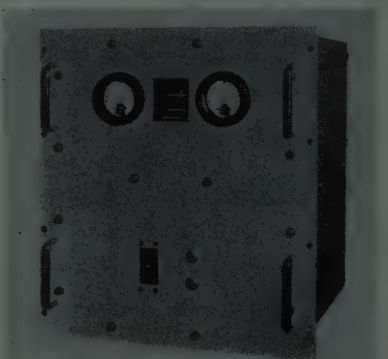
(Continued from page 108A)



on phase 1, 30/15 volts center tap control on phase 2, stall power input of 3.0 watts per phase, 0.3 ounce/inch torque at stall, a no load speed of 6500 RPM, and a stall current of 0.15 amperes on phase 1 and 0.121 amperes on phase 2. Generator excitation is 26 volts, 400 cps 3.0 watts. Generator output is 0.25 volt per 1000 RPM, null voltage 0.015 total, wobble voltage 0.007 maximum, linearity $\frac{1}{2}$ per cent to 4000 RPM, phase shift $0^\circ \pm 10^\circ$.

Transistorized DC Power Supply

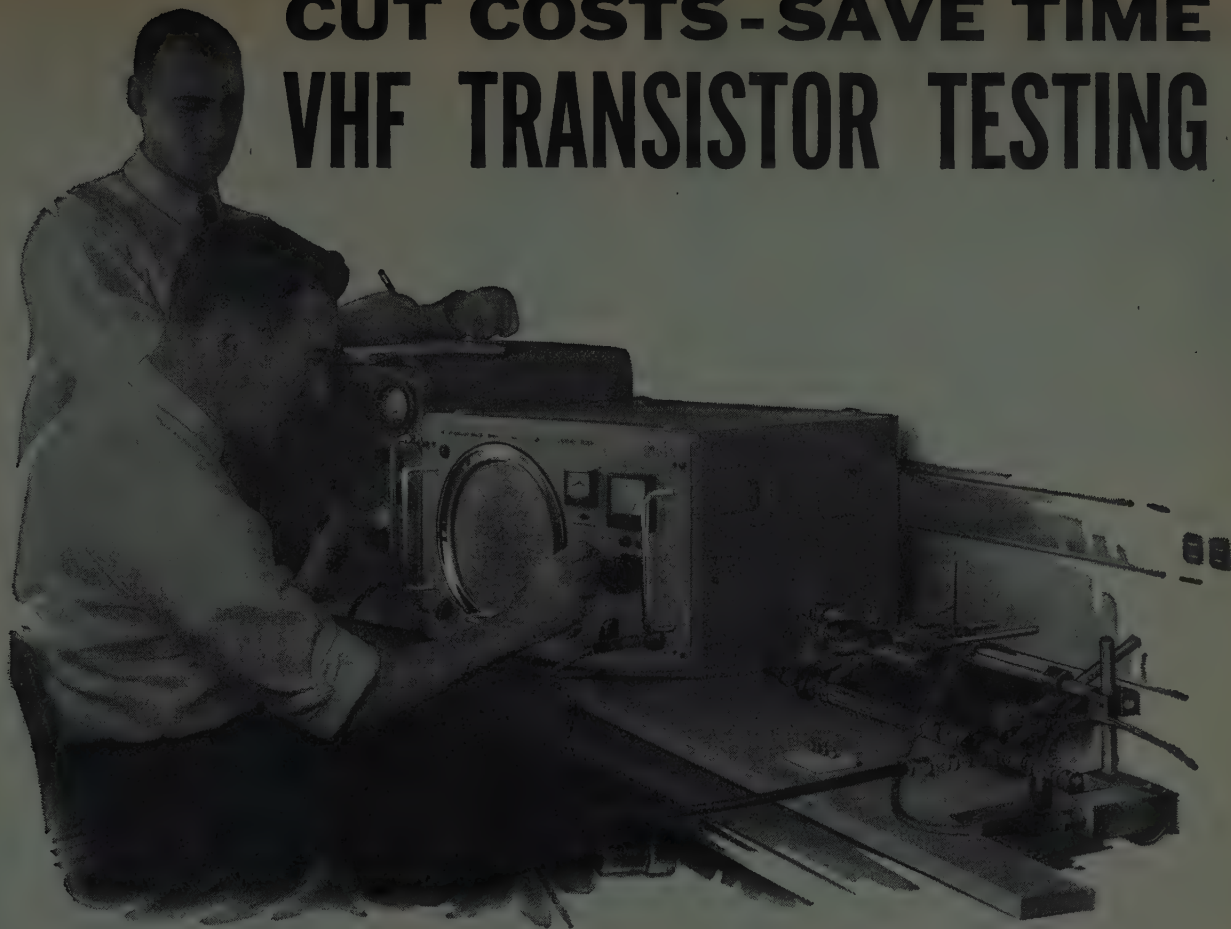
Development of a 24-32 volt at 100 ampere, completely transistorized and militarized, dc power supply has been announced by Perkin Engineering Corporation, 345 Kansas Street, El Segundo, Calif.



This completely new Power Supply designated Model No. M-1136A, operates from an ac input of 208 volts ± 10 per cent, 3 phase, 57-63 cps. The unit provides 24-32 volts at 100 amperes and has a dc current overload capacity of 125 amperes for a duration of 15 minutes. The static regulation accuracy is ± 0.1 per cent for line changes from 187-299 volts ac and ± 0.1 per cent for changes from no load to full load. Dynamic regulation is ± 0.1 per cent for step changes of 10 volts in the ac line between 187 to 229 volts and dynamic load regulation is ± 2 volts for step changes from no load to full load or full load to no load. The output impedance is less than

(Continued on page 112A)

CUT COSTS - SAVE TIME VHF TRANSISTOR TESTING



Engineers at Bell Telephone Laboratories measure transistor characteristics. From left, equipment includes signal generator, Federal's Diagraph and special coaxial jig set-up.

Eliminate Costly Adjustments, Calibrations and Conversions . . .

Leading transistor developers and manufacturers save valuable engineering time with the Federal Diagraph*. Complex reflection coefficients, impedance and other transmission characteristics are measured by simple adjustments of three controls. No recalibrating is needed to measure at different frequencies across the band. Set-up time is cut to a minimum . . . complex calculations and conversion tables eliminated. Data are read directly from any of five interchangeable charts suitable for filing or reproduction. Save supervision time . . . technicians can operate the Federal Diagraph with greater accuracy due to the inherent simplicity of measurement and the built-in "self-checking" system.

* Manufactured by Rohde & Schwarz

** Complete original paper available on request.

For high-frequency transistor testing as well as general two and four terminal measurements on coaxial systems—production or laboratory—routine or development—get greater flexibility and efficiency over a longer period of time with the Federal Diagraph.

Write for additional application data.** Live demonstrations of the Diagraph are available by special request on company letterhead.

SPECIFICATIONS

TWO MODELS IN STOCK: FT-ZDU 30 to 300 mc; FT-ZDD 300 to 2400 mc.

CHARACTERISTIC IMPEDANCE: 50 ohms.

MEASURING RANGE: Impedance . . . 1 to 2500 ohms;
Phase . . . 0 to 360°; Attenuation . . . 0 to 30 db.

ACCURACY: Amplitude . . . $\pm 3\%$; Phase $\pm 1.5^\circ$.

TERMINALS: Type N.

POWER SUPPLY: 115 volts (or 220 volts), 50 to 60 cycles.

DIMENSIONS: 22" x 14" x 19".

WEIGHT: 135 pounds.

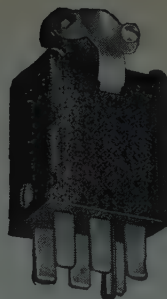
ITT

Industrial Products Division

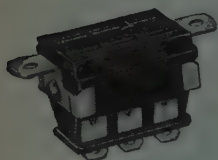
INTERNATIONAL TELEPHONE AND TELEGRAPH CORPORATION—250 GARIBALDI AVE., LODI, N. J.

FOR PUBLIC ADDRESS, RADIO, and kindred fields, **JONES 400 PLUGS & SOCKETS** SERIES

of proven quality!



P-406-CCT



S-406-AB

Double Contact Area

Phosphor bronze knife-switch socket contacts engage both sides of flat plug contacts.

Socket contacts phosphor bronze, cadmium plated. Plug contacts hard brass, cadmium plated. Insulation molded bakelite. Plugs and sockets polarized. Steel caps with baked crackle enamel. 2, 4, 6, 8, 10, 12 contacts. Cap or panel mounting.

Information on complete line, in Jones Catalog 22. Electrical Connecting Devices, Plugs, Sockets, Terminal Strips. Write



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(Continued from page 110A)

0.025 ohms from 0 to 20 kc and ripple is 20 millivolts RMS maximum.

The unit is contained in rack panel mount construction having dimensions of 19 wide×21 high×18 inches deep and the weight is approximately 200 pounds. Military specification meters per MIL-M-10304 "ruggedized" and hermetically sealed are mounted on front panel together with breakers and controls.

The unit is constructed using specification MIL-P-6457 and MIL-G-008512A as a guide in manufacture.

Additional information and complete specifications on the foregoing Power Supply can be obtained by requesting Perkin catalogue No. E-59.

Burns and Campion VP's of Siegler

Dan W. Burns and Robert T. Campion have been elected Vice Presidents of the Siegler Corp., of Los Angeles, Calif., by action of the Board of Directors, it was announced today by John G. Brooks, president.



Burns



Campion

Campion, who joined the electronics firm in 1957 as secretary of the corporation, will continue to hold that position along with his new title. Prior to joining Siegler, Campion was a partner in Alexander Grant & Co., certified public accountants, of Chicago, Ill.

Earlier this year, Burns was named President of The Hufford Corp., a Siegler subsidiary located in El Segundo, Calif. He had been serving previously as Vice President and General Manager of this manufacturer of special machinery for aircraft and missile firms. Burns' prior business experience included positions with various manufacturing, construction equipment and engineering firms.

50 KV DC Test Set

Designed for remote control of a compact 50 kv dc high voltage oil tank section, the control unit pictured here utilizes a new sloping front cabinet with a removable instrument panel which is set back to protect the components. The high voltage oil tank not shown here is a small unit on casters. An interconnecting cable connects the high voltage tank section with this control cabinet. Manufacturer is Peschel Electronics, Inc., Towners, Patterson, N. Y.

(Continued on page 114A)

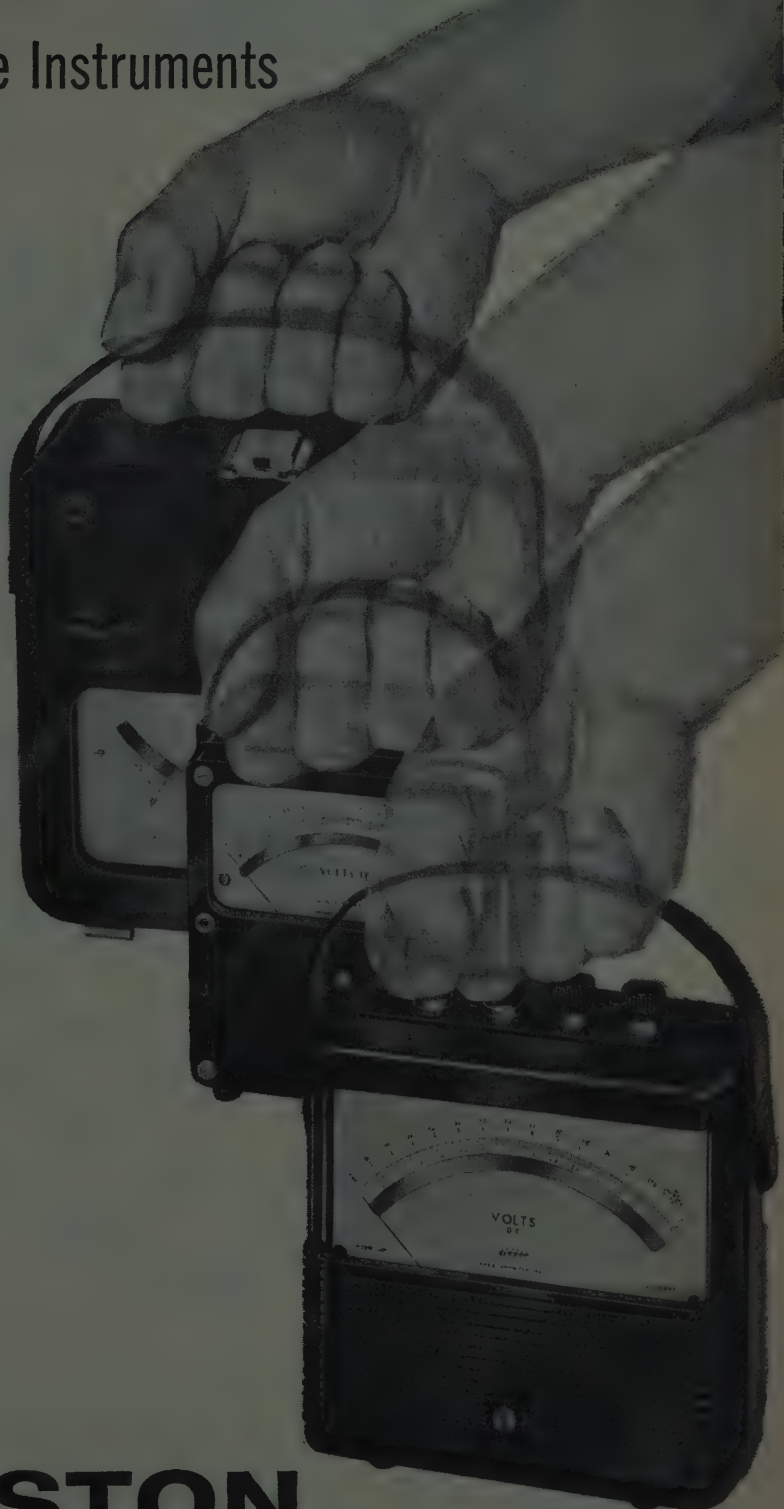
TOP ACCURACY IS AT YOUR FINGER-TIPS

...with Weston Portable Instruments

Easy portability, exceptional readability, sustained high accuracy... these features have been painstakingly engineered into every Weston Portable. Each is hand calibrated by direct comparison with precise reference standards. All are shielded against the effects of external magnetic fields... far in excess of ASA requirements. Weston Portables are equipped with long mirror scales and knife-edge pointers to eliminate parallax errors. All are well compensated for temperature changes.

Models 931, 901 and 622 make up a graduated series of Weston Portables. They cover a broad range of applications — from general testing in field, plant or laboratory to the exacting demands of electronics, telephony and temperature measurement. The 931 group and the 901 group have scale lengths of 4.0" and 5.5" respectively. The unusually sensitive '622' instruments have 6.1" scales, with proportionately greater accuracies and readability.

You'll find complete information in the Weston bulletins covering these instruments. Call your local Weston representative... or write to Weston Instruments, Division of Daystrom, Inc., Newark 12, N. J. *In Canada: Daystrom Ltd., 840 Caledonia Rd., Toronto 10, Ont. Export: Daystrom Int'l., 100 Empire St., Newark 12, N. J.*



WESTON

Instruments



For 2500 Bits Per Second Over Voice Communication Circuits . . . it's the **SEBIT-25**



The SEBIT-25 (shown above) is a transistORIZED transmit-receive unit for **SERIAL BINARY INFORMATION TRANSMISSION** up to 2500 baud in a nominal 3-kc voice band.

HOW THE SEBIT-25 OPERATES:

The SEBIT-25 uses vestigial sideband transmission and synchronous operation. This simple AM system includes time delay and amplitude distortion compensating circuits. **FIELD TESTS SHOW** that the unit can be operated successfully over wire lines several thousand miles long.

CHECK THESE POSSIBLE USES:

- ✓ High speed data transmission for business machines and computers
- ✓ High speed facsimile
- ✓ Transmission of time division multiplex information
- ✓ Sequential transmission of telemetering data

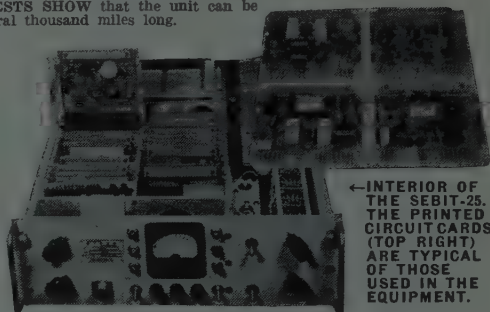
ADVANTAGES:

- Small size
- All solid state devices (no vacuum tubes)
- Ruggedness
- Low power consumption
- Simple, nonsophisticated circuitry

WRITE OR PHONE FOR TECHNICAL LITERATURE, PRICES, AND DELIVERY TIME.

RIXON ELECTRONICS INCORPORATED

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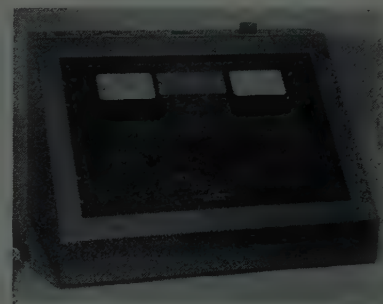


←INTERIOR OF THE SEBIT-25. THE PRINTED CIRCUIT CARDS (TOP RIGHT) ARE TYPICAL OF THOSE USED IN THE EQUIPMENT.



These manufacturers have invited **PROCEEDINGS** readers to write for literature and further technical information. Please mention your **IRE** affiliation.

(Continued from page 112A)



The complete test set—the above control cabinet and the high voltage section in an oil tank, is used for dielectric testing of insulation on large motors, generators, transformers, bushings, and high-voltage cable. It can perform non-destructive proof testing during production, final inspection, or preventive maintenance testing.

It is used for measuring leakage current in insulation at high voltages, for breakdown testing, or as a high-voltage power supply.

The control cabinet provides for dual-scale metering of both load current and output voltage, continuously adjustable output control from zero to 50 kv dc, a zero start interlock with optional bypass switch on the powerstat output control, usual switches with pilot lights, for input power and high-voltage, fuses, HV on and HV off push buttons with lock-in contactor, and a selector switch for either straight ground or guarded return. A fault relay deenergizes the high-voltage at the maximum capacity of the test set.

Features include filtered dc output, automatic meter protection, guard circuit to enable measurements of small leakage currents, 4 inch square meters with dual scales.

Available in ratings from 5 ma to 50 ma these test sets enable fast charging of highly capacitive loads, long cables, etc.

Requirements are 115 volts, 60 cps, single phase.

Silicon Solar Cells Brochure

A four-page brochure detailing the electrical and physical characteristics of the standard Hoffman line of silicon solar cells has just been published by the Semiconductor Div., Hoffman Electronics Corp., 930 Pitner Ave., Evanston, Ill.

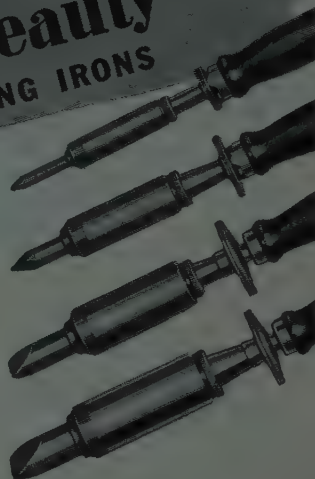
The new brochure (Technical Information Bulletin 32-58) gives complete design parameters as well as application notes on nine types of cells. Illustrated are spectral response curves, current-voltage characteristics at various light levels, variations of available power according to temperature, and a magnified view showing construction details of a typical solar cell.

(Continued on page 116A)

*EXPERIENCE SINCE 1894 Built into American Beauty ELECTRIC SOLDERING IRONS

***EXPERIENCE: "Knowledge, Skill, Or Technique Resulting From Experience."**

Since 1894 we have been designing, manufacturing and constantly improving our electric soldering irons! Today, no matter what the requirements, there's an American Beauty in the right model, correct tip size and proper watt input to do any soldering job quickly, properly, efficiently.



TEMPERATURE REGULATING STAND

An automatic device for controlling tip temperature while iron is at rest. Prevents overheating of iron and eliminates frequent retinning of tip, while at same time maintaining it at any temperature that may be desirable or necessary.

Write for 16-page illustrated catalog containing full information on our complete line of electric soldering irons—including their use and care.

AMERICAN ELECTRICAL HEATER COMPANY

DETROIT 2, MICHIGAN

172-G





IR

Today the Singer Manufacturing Company's Military Products Division is performing a substantial role in basic research and development, engineering and production of infrared systems and components. This is just one of many ways in which the Military Products Division—composed of H.R.B., Inc., Diehl Manufacturing Company, and Bridgeport—is now serving national defense. Write for complete details.



THE SINGER MANUFACTURING COMPANY
 Military Products Division • 149 Broadway, New York 6, N. Y.
HRB • DIEHL • BRIDGEPORT

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(Continued from page 114A)

The cells described are the same as those still powering a radio transmitter in the Vanguard satellite after seven months in space.

Inquiries for the brochure should be addressed to the firm.

Decommuration Equipment

New telemetry decommuration equipment that can handle sampling rates from 24 to 3600 pps in both Pulse Amplitude (PAM) and Pulse Width (PWM) coding is now in production at the Applied Science Corporation of Princeton, P.O. Box 44, Princeton, N. J.

The new equipment is a more compact and flexible version of ASCOP M-Series decommuration and display equipment which has been used in missile and aircraft development programs for the last seven years.

Besides the dual PAM/PWM capacity and the wide sampling rate capability, the new equipment also features:

Long term system accuracy of better than ± 0.5 per cent, including any system non-linearity and drifts.

An undecommutated but thoroughly corrected output for convenience in digitizing. This is in addition to a wide variety of corrected and separated analog voltage outputs.

The sampling rate capability makes the new equipment compatible with both standard IRIG configurations and a large number of non-standard rates. Non-standard rates are important for operation with new high speed electronic multiplexers and with faster-than-real-time playback of tape recorded data. They also insure that the equipment will meet the requirements of future telemetry developments.

The new M-Series design emphasizes flexible modularization. New M-Series chassis have a 7-inch modular front panel and can be mounted in all standard equipment racks.

Some important engineering features of M-Series decommuration ground stations are:

Automatic input shaping by signal slicing and clean reconstruction processes. This insures proper equipment operation under adverse signal-to-noise ratios.

Automatic sequence correction and synchronization. System will maintain

(Continued on page 118A)

STROMBERG-CARLSON Type "A" Relays with Plug-in mountings



For fast, easy removal and replacement you can get Stromberg-Carlson Type "A" Relays with *plug-in* mountings.

The Stromberg-Carlson Plug (illustrated above) automatically locks the relay in place and guarantees a low-resistance connection between plug and socket. Its 36 terminals provide enough connections for practically all relay applications. Coils and contacts are wired to terminals as your needs dictate. Contacts can be furnished in silver, palladium, gold alloy or palladium-silver alloy.

Spring combinations possible with this assembly are 17 Form A or Form B; 10 Form C or Form D.

Also available in an "A" Relay is a plug used with commercial radio type sockets. It can mount relays with 8, 9, 12 or 20 connections.

For technical details and ordering information, send for Bulletin T-5000R, available on request. Write to:



STROMBERG-CARLSON

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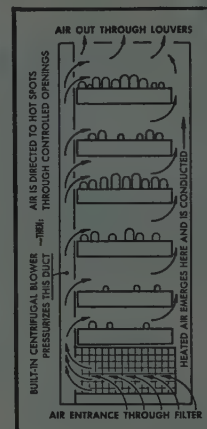
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S BAND FILTERS

Characteristics	Two (2) Section Resonator	Three (3) Section Resonator	Four (4) Section Resonator
Model No.	27-BW	27-CW	27-DW
Type of Resonator	TE ₁₀₁ mode rectangular	TE ₁₀₁ mode rectangular	TE ₁₀₁ mode rectangular
Tuning Range	2700-3150 MCS	2700-2950 MCS	2700-2900 MCS
3 db Bandwidth	4.5-6.5 MCS	4.5-5.5 MCS	4.5-5.5 MCS
Max 30 db Bandwidth	36 MCS	18 MCS	13 MCS
Max Insertion Loss	.9 db	1.3 db	1.8 db
Price	\$400.00	\$535.00	\$670.00
Model No.	27-BC	27-CC	27-DC
Type of Resonant Cavity	$\lambda/4$ coax	$\lambda/4$ coax	$\lambda/4$ coax
Tuning Range	2700-3200 MCS	2700-3100 MCS	2700-2950 MCS
3 db Bandwidth	8-11 MCS	8-10 MCS	8-9 MCS
Max 30 db Bandwidth	60 MCS	32 MCS	21 MCS
Max Insertion Loss	1.6 db	2.4 db	3.2 db
Price	\$350.00	\$475.00	\$600.00

C BAND FILTERS

Characteristics	Two (2) Section Resonator	Three (3) Section Resonator	Four (4) Section Resonator
Model No.	54-BC	54-CC	54-DC
Type of Resonator	$\lambda/4$ coax	$\lambda/4$ coax	$\lambda/4$ coax
Tuning Range	5400-5950 MCS	5400-5950 MCS	5400-5750 MCS
3 db Bandwidth	8-11 MCS	8-10 MCS	8-9 MCS
Max 30 db Bandwidth	60 MCS	32 MCS	21 MCS
Max Insertion Loss	2 db	3 db	4 db
Price	\$360.00	\$485.00	\$610.00

L BAND FILTERS

Characteristics	Two (2) Section Resonator	Three (3) Section Resonator	Four (4) Section Resonator
Model No.	96-BC	96-CC	96-DC
Type of Resonant Cavity	$\lambda/4$ coax	$\lambda/4$ coax	$\lambda/4$ coax
Tuning Range	960-1150 MCS	960-1100 MCS	960-1050 MCS
3 db Bandwidth	8-11 MCS	8-10 MCS	8-9 MCS
Max 30 db Bandwidth	60 MCS	32 MCS	21 MCS
Max Insertion Loss	1.2 db	1.8 db	2.5 db
Price	\$370.00	\$495.00	\$620.00

X BAND FILTERS

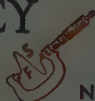
Characteristics	Two (2) Section Resonator	Three (3) Section Resonator	Four (4) Section Resonator
Model No.	75-BW	75-CW	75-DW
Type of Resonant Cavity	TE ₁₁₁ mode cylindrical	TE ₁₁₁ mode cylindrical	TE ₁₁₁ mode cylindrical
Tuning Range	7500-8500 MCS	7500-8250 MCS	7500-8000 MCS
3 db Bandwidth	8-11 MCS	8-10 MCS	8-9 MCS
Max 30 db Bandwidth	60 MCS	32 MCS	21 MCS
Max Insertion Loss	1.5 db	2.5 db	3.5 db
Price	\$475.00	\$625.00	\$775.00
Model No.	85-BW	85-CW	85-DW
Type of Resonant Cavity	TE ₁₁₁ mode cylindrical	TE ₁₁₁ mode cylindrical	TE ₁₁₁ mode cylindrical
Tuning Range	8500-9600 MCS	8500-9300 MCS	8500-9000 MCS
3 db Bandwidth	8-11 MCS	8-10 MCS	8-9 MCS
Max 30 db Bandwidth	60 MCS	32 MCS	21 MCS
Max Insertion Loss	1.5 db	2.5 db	3.5 db
Price	\$475.00	\$625.00	\$775.00

All of the above filters have Max VSWR of 1.5, and either a single shaft or counter dial for Tuning Control. Depending upon mode of operation, units are supplied with either Type N Connectors or Waveguide flanges.

DELIVERY IN 90 DAYS

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A DIVISION OF



NATIONAL ELECTRIC PRODUCTS CORP.

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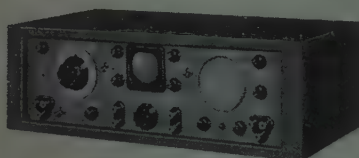
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WHY NOT USE THEM!

The standard time and frequency transmissions of the National Bureau of Standards radio stations WWV and WWVH provide an invaluable service to laboratories and experimenters throughout the world. Extremely precise (normal transmission stability is within 1 part in 10^9 at WWV and 5 parts in 10^9 at WWVH) audio and radio frequency standards, as well as accurate time intervals and radio frequency propagation warnings, are placed at the disposal of anyone having a receiver capable of tuning to one or more of the transmitting frequencies. Proper use of these facilities can be made to supplement the instrumentation of any laboratory.

The Model WWVC Standard Frequency Comparator is just such an instrument . . . a highly sensitive crystal-controlled radio receiver utilizing WWV and WWVH transmissions.



MODEL WWVC COMPARATOR

A 5-position dial switches *precisely* to any Standard Frequency—2.5, 5, 10, 15, or 20MC. It features built-in oscilloscope and speaker, comparator function selector, Collins plug-in filter for high selectivity, automatic gain and volume controls and adjustable threshold control which eliminates noise and other modulation in tick position.

Send for bulletin #557, "Using Standard Time and Frequency Broadcasts"



SPECIFIC PRODUCTS

Box 425, 21051 Costanso
Woodland Hills, Calif.



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(Continued from page 116A)

sync through 8 sequential missing pulses with a simultaneous change in sampling rate of -20 per cent from nominal.

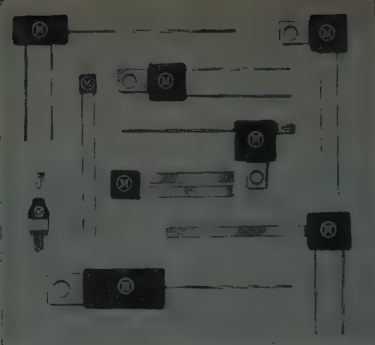
Automatic and continuous correction by reference of the multiplexed data train to stable full-scale and zero reference channels.

All basic M-Series units can handle up to 100 channel signals, with 30, 45, 60 and 90 as standard channel configurations. A basic PAM/PWM unit is 35½ inches high and 19 inches wide and consists of an Input Shaper, Channel Selector, Control Translator, Output Converter and Power Supply. A wide range of optional units can be added, including signal simulators, meter readout units, pen recorders, monitor oscillographs and digital voltmeters.

New Capacitor Lead Arrangements

In order to achieve greater dimensional versatility subminiature ceramic capacitors are now available in a wider variety of lead arrangements in any one of the twelve ceramic materials from Mucon Corp., Dept. K, 9 St. Francis St., Newark 5, N. J.

These ceramics offer a greater choice of



sizes, temperature ranges, and characteristics to the designer working with higher capacitances and more critical space limitations, as well as lower lead inductance requirements. There are an unlimited selection of wire, ribbon or tab terminals which may be had in any desired number, thickness or configuration to provide the best circuit arrangement.

The ceramic elements may also vary from square to rectangular, with thicknesses as little as 0.065 inch. Two or more ceramic elements may be stacked in parallel for higher capacitance.

Applications include transistor circuitry, missiles, hearing aids, computers, radio and TV, filters, radar and uhf.

(Continued on page 120A)

**Radio Engineering
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March 23-26, 1959
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TEST STAND
OPERATION



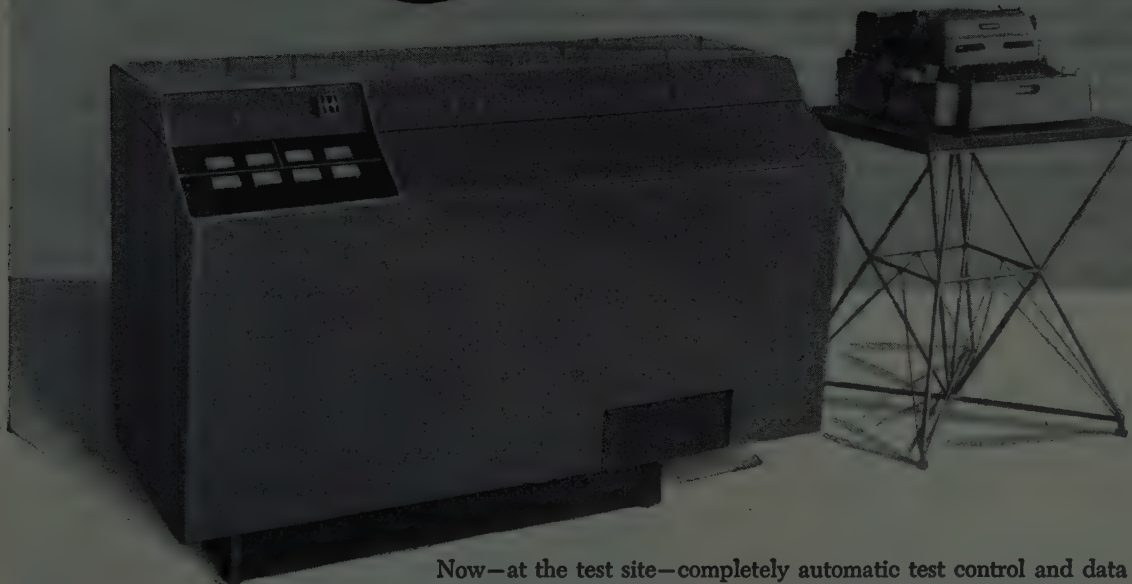
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INSTRUMENTATION



TELEMETRY
DATA REDUCTION



The RW-300
is the first
digital computer
for test control
and data reduction



Now—at the test site—completely automatic test control and data reduction can be handled by a single system incorporating the Ramo-Wooldridge RW-300 Digital Control Computer. The new RW-300 can schedule and closely control test routines, and it can collect, analyze, and record test data.

The versatile RW-300 utilizes input data as feedback to modify control actions, thus substantially shortening many test routines. In addition, the RW-300 directly logs both instrument data and complex relationships among these data. Thus, test results are available immediately. The time-consuming task of processing raw data through a separate computer, often remote from the test facility, usually can be eliminated.

For technical information on automatic test control and data reduction with the RW-300 and with special digital systems which utilize solid-state components exclusively, write: Director of Marketing, The Thompson-Ramo-Wooldridge Products Company, P.O. Box 90067, Airport Station, Los Angeles 45, California, or call OSborne 5-4601.

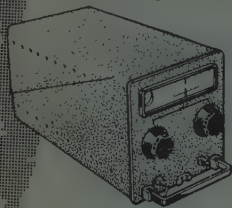


THE THOMPSON-RAMO-WOOLDRIDGE PRODUCTS COMPANY

AWA

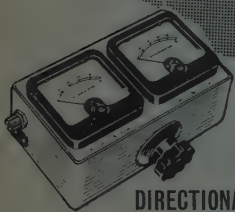
ELECTRONICS

New concepts in electronics have been developed at AWA, as a result of experience with missile systems. Now they have a wider application. Here are some of the new AWA devices now available to industry.



U.H.F. WIDEBAND RECEIVER

Basic arrangement consists of R.F. amplifier, mixer, local oscillator, I.F. amplifier (A.G.C. controlled), cathode follower output stage. Tuning indicator (EM 34) is also fitted to receiver. The standard forms: one for airborne racking with special separate power supply unit, the other on larger chassis including power supply unit (conventional 19" front panel). Standard specification: 420-470 M/cs frequency range; 4 M/cs overall bandwidth, approximately 10 db noise factor; approximately 70 ohms input impedance, 200-250 V and 50-60 c/s input supply. Input is unbalanced, output is via low impedance (cathode follower) stage.



DIRECTIONAL COUPLER

Of the 'Loop' type, suitable for measurements of RF power and Standing Wave Ratio in coaxial cables. Directional properties are largely unaffected by frequency changes, so coupler may be used to help obtain optimum termination of a 52 ohm coaxial system up to 600 M/cs. Standard specification: Size 7" x 4" x 2 1/4"; weighs 4 lbs. 3 ozs.; Power Measurement Range is Low range 1w.cw.max. High range 5w.cw.max.; less than 1% attenuation; better than 2% accuracy at frequency of calibration.

All devices are adaptable to suit customers' own requirements. For further information consult:

COMMERCIAL ELECTRONICS DEPT.

SIR W. G. ARMSTRONG WHITWORTH AIRCRAFT LTD.
Baginton, Coventry, England

MEMBER OF THE HAWKER SIDDELEY GROUP



NEWS New Products



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(Continued from page 118A)

Automatic TV "Flyback" Tester

As a solution to economical parameter investigation, a new completely automatic horizontal output transformer (flyback) tester has been put into operation at the F. W. Sickles Division of General Instrument Corp., Engineering Department, Chicopee, Mass.

The operator has no meters to read or decisions to make, but merely inserts the flyback to be tested into a fixture and pushes a button to start the test. The flyback is automatically put through a complete test cycle. At the completion of the cycle a "good" or "reject" light indicates the test result. Limits can be set on all parameters so that anything falling outside the preset limits will cause the reject light to come on. In addition to the reject light there are 15 additional lights, one or more of which will come on indicating the particular part of the test cycle the unit failed to pass. Design of the equipment allows a full test cycle to be made even if a reject condition is encountered, with the exception of an overload in which case the test stops at that moment.

(Continued on page 122A)

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ELECTRONICALLY SWEPT BACKWARD WAVE OSCILLATORS



**FREQUENCY
RANGE**
0.5 TO
18.0 KMC

A complete unit consists of a universal sweeping supply with an oscillator head. The modular design permits coverage of the entire range of 0.5 to 18.0 kmc with a single supply.

M P E

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PLEASE WRITE FOR COMPLETE SPECIFICATIONS

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producing **INTEGRATED AIRCRAFT ANTENNA SYSTEMS**..from concept to roll-out



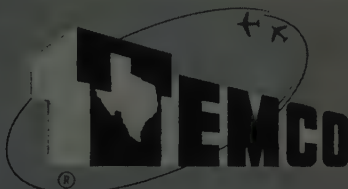
Designing and producing high performance aircraft antenna systems calls for highly developed skills and advanced techniques. But the key to their successful operation is integration of the antenna into the airframe. At Temco, proven airframe and antenna engineering capabilities unite to produce optimum performance integrated airframe-antenna systems.

Many Temco-developed antenna systems are already operational, principally in reconnaissance and electronic counter-measures applications. These systems include equiangular and Archimedes spirals, slots and radiating cavities for flush installations . . tapered helices, discones, stubs and horns . . operating in up to 5:1 bandwidths. Advanced production

techniques at Temco . . etched-circuit methods, high-strength plastic fabrications, precision calibration . . are skills evolved through experience, and implemented in complete, modern facilities.

With its Antenna Research Laboratory and new precision Test Range, Temco is keeping a step ahead of today's high-performance aircraft and missiles. New antenna-airframe designs are under development for operation from 30 MC to beyond 30,000 MC. Integrated antenna systems . . designed and produced by Temco for aero-space craft electronics . . are indicative of Temco's system of weapons management. In subcontracts . . or complete systems, Temco's capabilities are ready to meet your challenge.

Tomorrow's need is today's challenge at . .



AIRCRAFT CORPORATION • DALLAS, TEXAS

This Small Lever Action Switch Requires Minimum Depth Behind the Panel!



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(Continued from page 120A)

Another **SWITCHCRAFT[®] INC.** *First*

**SERIES 12000
"LEV-R SWITCH"**

Available in Two Position and Three Position Types, Locking and Non-locking; also Three Position Locking one side — Non-Lock other side. Standard circuits.

Diagram labels: FINE SILVER CONTACTS, VARIABLE DEPENDING ON CIRCUIT, -32 NEF THREADS, APPROX. 30°, INSULATOR.

Requires only about 1/4 of depth of conventional "Key" switches, behind the panel. Single hole mounting.

Relatively long springs without any "forms" at point of flexing insures suitable spring action for long life.

Fine silver contacts, rated at 3 amps. (300 watts max.) non-inductive load, are standard. Special circuits and Palladium contacts for low-current low-voltage circuits available on special order.

Write for Bulletin S-593.

SWITCHCRAFT[®] INC.

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Canadian Rep.: Atlas Radio Corp., Ltd., 50 Wingold Avenue, Toronto, Ontario

AVAILABLE AT ALL LEADING RADIO PARTS JOBBERS •

**MODEL 2S
X-Y- \bar{T} *
RECORDER**

11" x 17" Recording Table (Vacuum Grip)

Y = 5 mv to 500 volts

X = 7.5 mv to 500 volts (or) 7.5 to 750 seconds

with TIME BASE

THE MOSELEY

AUTOGRAF

A DIRECT WRITING, LOW FREQUENCY OSCILLOGRAPH for:

- X-Y RECORDING — Automatically draws curves directly from a variety of electrical data.
- CURVE FOLLOWING — With adaptor, regenerates functions from original curves traced with conducting ink.
- POINT PLOTTING — Plots points directly from Keyboard; with translator, plots from Card Punch or Tape Reader.
- FUNCTION vs TIME — Automatically plots dependent variable against TIME. (5 Sweep Ranges)

Send for detailed specifications:

F. L. MOSELEY CO.

409 N. FAIR OAKS AVENUE, PASADENA, CALIFORNIA



The machine automatically performs the following tests:

Test 1. Tap Test. Each connection of the flyback is individually checked for continuity and correct number of turns.

Test 2. Optional Voltage Test. Measurements are made of scan or width, cathode current of the driver tube and recovered high voltage while the "flyback" is operated under normal conditions.

Test 3. Overvoltage Test. Measurements are made of scan or width, cathode current of the driver tube and recovered high voltage while the "flyback" is operated under over-voltage or breakdown voltage conditions.

Tests Up to 12 Taps

During Test 1, a sine wave signal is applied to the "flyback." Each of the induced tap voltages is then fed, one at a time, through a constant gain amplifier to a magnetic amplifier indicating circuit. The machine is capable of testing up to 12 taps although the normal flyback has only 3 to 5 taps; the additional provisions are mainly for color "flyback" transformers. Individual adjustments permit the use of one magnetic amplifier indicating circuit for all 12 taps. The time that each tap is tested is adjustable from zero to six seconds, the normal time being one and one-half seconds. A selector switch is preset to the number of taps to be tested on any one "flyback." The machine automatically goes into Test 2 when Test 1 is completed.

Adjustments for B+ supply voltage and drive are provided and preset so that during Test 2 the "flyback" will be tested under normal operating conditions. Precision measurements are made of scan or width, driver cathode current and recovered high voltage through use of three magnetic amplifier indicating circuits. The elapsed time for Test 2 is adjustable.

Upon completion of this test the machine automatically goes into Test 3.

(Continued on page 126A)



In Development Engineering—meet two men who get results

Hunting ducks or developing military systems ... teamwork pays off

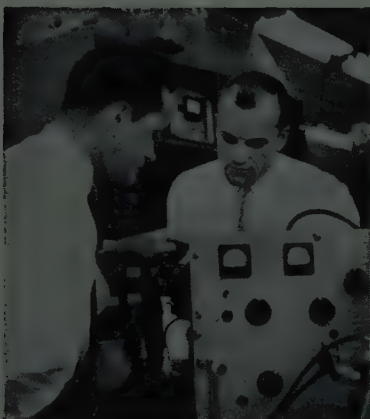
Sighting his bird is Ken Coon, manager of the Guidance and Navigation Laboratory at the Mechanical Division of General Mills. The second nimrod is Murray Harpole, manager of our Communications and Control Laboratory.

In a duck pass, these engineers cooperate to bring home the bag limit. At the plant, they cooperate to transform ideas into reality.

Their engineering groups work independently, each with clearly defined areas of responsibility but each recognizing an essential interdependence.

This broad, overall awareness of "target" and the cooperative method of achieving it are the *plus capabilities* which enable General Mills to produce military systems and sub-systems to the strictest specifications—in the shortest possible time.

NEW BOOKLET RIGHT OFF THE PRESS tells and shows the many ways we serve industry and the military. Write for your copy. Address Dept. PI-12.



Here Mr. Harpole and Mr. Coon check out the Radar Systems Tester recently developed by General Mills. Both men are Registered Professional Engineers. Each has an impressive record of achievement in his special fields. Coon and Harpole—two more of the many good reasons our customers say, "At General Mills, we get results."

MECHANICAL DIVISION

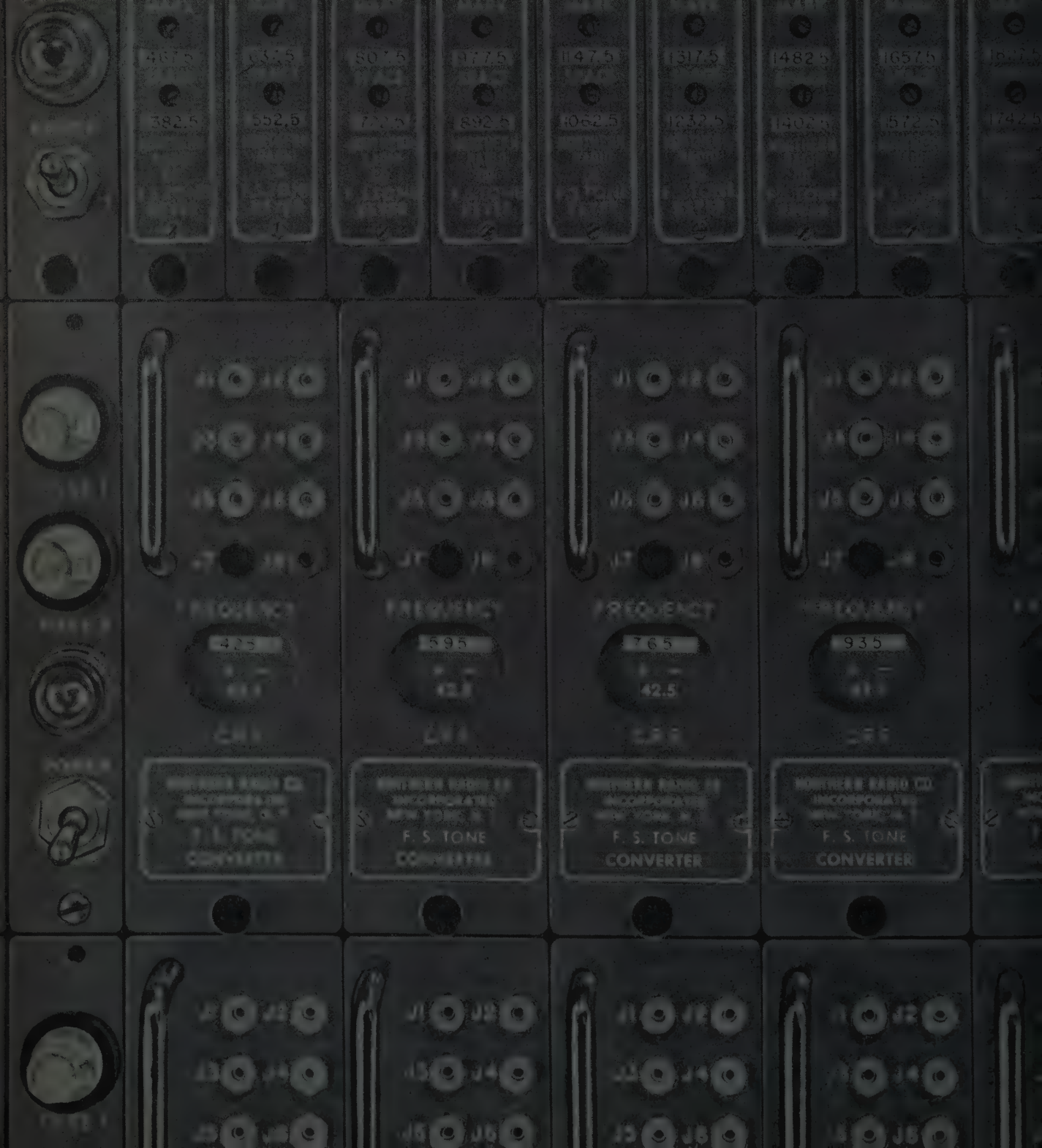
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Transmitters—18 Channels—Now $\frac{1}{12}$ Former Size



ACTUAL SIZE!

Receivers—18 Channels—Now $\frac{1}{6}$ Former Size

Voice Frequency Carrier Telegraph System
... the most MINIFIED of them all

NORTHERN RADIO

Transistorized

**18 channels in
only $15\frac{3}{4}$ " panel space**

Top shelf shows 18 Frequency Shift Tone Keyers, Type 211 Model 1;
Next 2 shelves contain 9 each Frequency Shift Tone Converters, Type 212 Model 1;

FREQUENCY SHIFT TONE KEYS—Type 211 Model 1
Keying inputs, levels & impedances: 1. Contact keying (internal battery to "dry" contacts) 1 ma. min.; 2. DC current pulses, positive or negative, neutral or polar, high range, 220 ohms, 30 ma. min. low range, 2200 ohms, 0.5 ma. min.; 3. DC voltage pulses, positive or negative, neutral or polar, high range, 100,000 ohms, 10 volts min., low range, 2200 ohms, 1 volt minimum.
Frequency Stability: Standard Networks ± 2 cps total for all causes including $\pm 10\%$ line voltage change and $\pm 25^\circ\text{C}$. from 25°C . temperature change.
Harmonic Content: All harmonics of the tone are more than 50 db below output level.

Output Frequencies: All standard VF carrier channels from 425 to 3315 cps. Bandwidth dependent on keying speed requirements. Other frequencies and bandwidths available on special order.
Output Level & Impedance: 5 dbm maximum, into 600 ohms, unbalanced. May be paralleled with any number of other keys operating on different frequencies in the same audio system.

Power Requirements: 14 V DC, 15 MA. Two transistorized power supplies and one automatic change-over relay are mounted on the rear of each mounting shelf.
Dimensions: $\frac{7}{8}$ " wide x $5\frac{1}{4}$ " high x $10\frac{1}{2}$ " deep.

FREQUENCY SHIFT TONE CONVERTER—Type 212 Model 1
Input Level & Impedance: -48 dbm to $+8$ dbm into 600 ohms, unbalanced. May be paralleled with any number of other converters operating on different frequencies in the same audio system.
Input Frequencies: All standard telegraph VF channels from 425 to 3315 cps. Bandwidth dependent on keying speed requirements. Other frequencies and bandwidths available on special order.

Output: Neutral DC voltage pulses of 10 volts maximum across a 2000 ohm external load. Polar pulses ± 10 volts across a 2000 ohm external load. Output drives appropriate voltage-to-current converters, such as Northern Radio Type 213 Transistor Relay, which provides proper teleprinter operating currents. Printers which are already equipped with internal repeating relays may be driven directly from the normal output terminals of the Type 212 Converter when so desired.
Power Requirements: 14 V DC at 30 MA. Two transistorized power supplies and one automatic change-over relay are mounted on the rear of each mounting shelf.

Dimensions: $1\frac{7}{8}$ " x $5\frac{1}{4}$ " x $11\frac{3}{4}$ " deep. For rack mounting a number of these units, a shelf assembly is available accommodating nine (9) units in a panel height of $5\frac{1}{4}$ ".

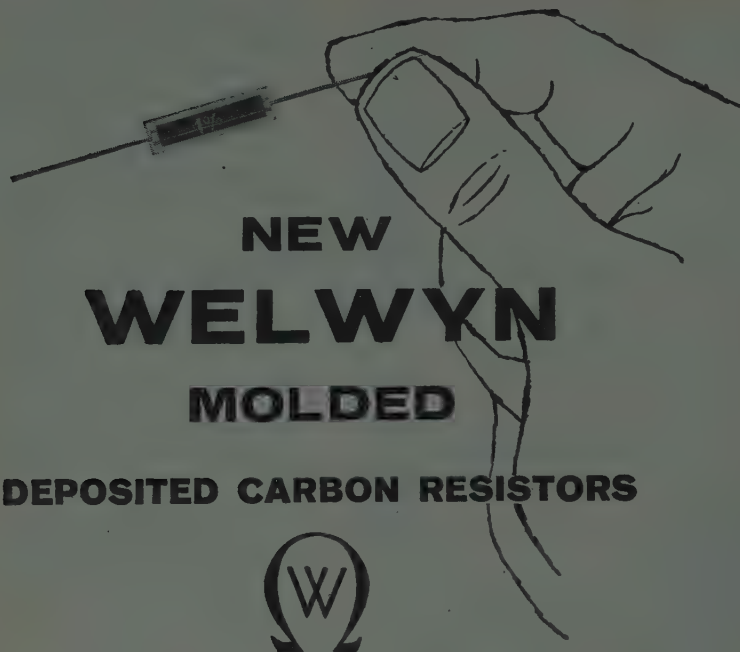
Write for complete technical data.

NORTHERN RADIO CO., INC. 147 W. 22nd Street, New York 11, N. Y.
Pace-Setters in Quality Communications Equipment

In Canada: Northern Radio Mfg. Co., Ltd., 1950 Bank St., Billings Bridge, Ottawa, Ontario

*Illustrated: 86.84% of actual width, 71.43% of actual height.

REDUCE BREAKDOWN FAILURES



The use of a thermo-plastic insulation material has resulted in an economically priced molded carbon resistor of markedly improved endurance and long term stability.

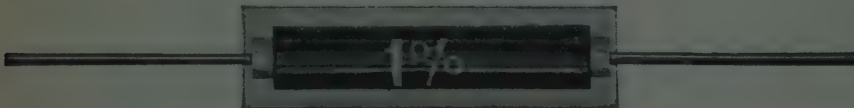
Type N resistors subjected to several one-hour cycles of immersion in boiling water — while DC polarized — have revealed only negligible changes in resistance. Continuous operations at 150°C caused no damage to the component.

The new Type N resistor, a deposited carbon film fired onto a porcelain rod, is first tropicalized with multiple coatings of pancratic lacquers to give it long term moisture resistance, and is then molded in a thermo-plastic material.

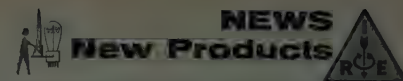
This molded insulation has an effective resistance in the order of 10^{13} ohms. Its inherent thermal conductivity is approximately ten times that of air, resulting in substantially improved load life under conditions involving excessive or high wattage dissipation. Similarly, Type N resistors may be soldered as close to the insulation as desired without fear of melting or deforming the cover.

One added advantage of the Type N is that the original markings on the resistor body remain visible and legible through the transparent molded material.

Welwyn Type N carbon resistors meet the requirements specified by MIL-R-10509B, and are available in all values, ranging from 10 ohms through 1 megohm. For complete data and specifications write to Welwyn International, Inc., 3355 Edgecliff Terrace, Cleveland 11, Ohio.



SAMPLES AVAILABLE ON REQUEST.



These manufacturers have invited PROCEEDINGS readers to write for literature and further technical information. Please mention your IRE affiliation.

(Continued from page 126A)

purpose use, are suitable for outdoor environments and airborne applications. The units are completely pressurized. Write to the firm for Technical Bulletin B-300.

Slow Scan Vidicon

A new small-size vidicon camera tube (WL-7290) designed for slow speed scanning operations is now available from the Westinghouse Electric Corp., Electronic Tube Div., P.O. Box 284, Elmira, N. Y.



The low residual current of this tube permits high resolution, long-storage time with higher sensitivity, higher output signal and better signal-to-noise ratio.

The WL-7290 is also useful for transmitting high resolution information over conventional audio circuits as the system bandwidth requirements are sharply reduced with slow scan.

In the ordinary vidicon, it is undesirable for the picture to remain on the storage surface for any appreciable length of time, since this would cause loss of detail, or smearing of the image. The WL-7290, however, has the characteristic of being able to store or "freeze" this image for several minutes, provided the surface is not scanned by the beam during this time. A high-quality picture, 350 line resolution, can be held for two minutes.

The WL-7290 is thus most applicable where a narrow bandwidth signal is desired and is obtained by a very slow scan.

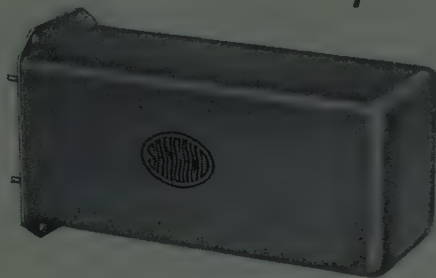
For further information, write to Westinghouse.

(Continued on page 146A)

Do You Have Critical Filter Problems?

Sangamo Electric Company has been designing and building specialty filters since 1927. These filters have been used in a wide variety of metering, telephone and military equipment produced by Sangamo, and by a limited group of electrical and electronic manufacturers. Sangamo's thirty years of filter design and manufacturing experience is now available to the industry.

SANGAMO
MAY HAVE THE
ANSWER TO YOUR
PROBLEM



Here's a Typical Example: The filter illustrated was required for use in a circuit which was designed to amplify extremely small signals in the range of 25 KC to 26 KC.

BASIC OPERATIONAL AND DESIGN SPECIFICATIONS:

Meet applicable requirements for military apparatus.

Operate in a plate circuit of an amplifier presenting an effective generator impedance of 47,000 ohms and to drive the grid circuit of the following amplifier stage.

Operate at signal level as low as 10 microvolts.

Must be well shielded against external fields.

Passband ripple not to exceed 1 db. from 25 KC to 26 KC.

Minimum rejection shall be 35 db. at 28 KC and 40 db. at 23 KC.

The phase shift, from one production filter to another, shall not vary more than 5° at any point in the 25 KC to 26 KC bandpass.

The phase shift and attenuation

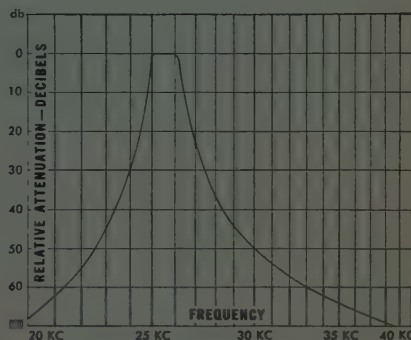
characteristics must be reproducible over a long period of years to insure properly functioning spare parts.

Temperature range 0° to 85°C.

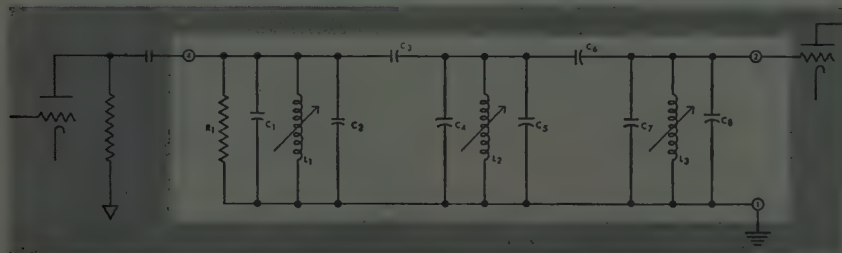
SANGAMO SOLUTION TO PROBLEM

The above requirements were met by using three parallel tuned circuits properly coupled by capacitors. Selection of the L-C ratios, coupling, and circuit Qs were made in order to fulfill the overall response requirements and at the same time present the proper load to the driving amplifier stage. Stability requirements were obtained by using Sangamo silvered mica capacitors. Negative temperature coefficient capacitors were inserted in parallel with the tuned circuits to correct for the positive temperature coefficient of the inductors. A phase shift variation of 2.5° maximum from 25 KC to 26 KC has been consistently maintained during eight years of production on these units. The

universal wound coils are enclosed in powdered iron cups with moveable slugs for precise adjustment of the response and the phase shift. These inductors manufactured by Sangamo have uniform distributed capacity and Q. The cup-enclosed inductance coils are in turn housed in a die-cast aluminum enclosure. This housing lends physical rigidity to the coupled structure and assists in minimizing magnetic interaction between the enclosed inductors. The entire filter assembly is enclosed in a hermetically sealed drawn steel case. The terminals are of the extremely rugged compression glass type.



Relative response curve of this Sangamo bandpass filter.



C₁, C₄, C₇—Temperature Compensators
C₂, C₃, C₅, C₆, C₈—Sangamo Silvered Mica Capacitors

Write us today for an engineering analysis of your specialized filter applications. Sangamo's engineers are ready to help you.



SANGAMO ELECTRIC COMPANY
SPRINGFIELD, ILLINOIS

6C58-5

MISSILES ARE BIG IN THE MIDDLE WEST, TOO!

... and there's big opportunity at BENDIX—prime contractor for the TALOS MISSILE

If you have the qualifications, you can build yourself an enviable engineering career with Bendix—and enjoy living in one of America's fine residential and recreational areas.

Bendix Missiles has opportunities now for engineers of exceptional ability. You'll be in the technical forefront of your profession at Bendix, working with men who have sparked some of the most important technological achievements of our

time. You'll have the use of facilities and equipment that are unmatched.

You'll enjoy a pleasant four-season climate, have excellent educational facilities available to you and your family, and have easy access to Chicago. Most of all, you'll find satisfaction in doing important work alongside men who are professional engineers. Mail the coupon today for a copy of "Opportunities Abound at Bendix Missiles".

Bendix Products Division—Missiles
402S So. Beiger St., Mishawaka, Ind.

Gentlemen: I would like more information concerning opportunities in guided missiles. Please send me the booklet "Opportunities Abound at Bendix Missiles."

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ADDRESS _____

CITY _____ STATE _____



By Armed Forces Veterans

In order to give a reasonably equal opportunity to all applicants and to avoid overcrowding of the corresponding column, the following rules have been adopted:

The IRE publishes free of charge notices of positions wanted by IRE members who are now in the Service or have received an honorable discharge. Such notices should not have more than five lines. They may be inserted only after a lapse of one month or more following a previous insertion and the maximum number of insertions is three per year. The IRE necessarily reserves the right to decline any announcement without assignment of reason.

Address replies to box number indicated, c/o IRE, 1 East 79th St., New York 21, N.Y.

ELECTRONIC ENGINEER

Liaison Engineer engaged in contractual and technical administration of multi-million dollar subcontract desires position in project administration or liaison. BBA, MBA. 8 years diversified electronic experience including test equipment design and system engineering. Schooled in military electronics. Box 1070 W.

ENGINEER

7 years transformer experience including design, production, test and the writing of specifications for transformers and their materials. Special experience in EPOXY resin embedment and in close tolerance reactor work. Box 1071 W.

ELECTRONICS EXECUTIVE

Graduate with 12 years experience in communications and controls. Leader. Desires challenge. Box 1072 W.

ELECTRONIC ENGINEER

Age 26. BSEE. 1954; MSEE. 1956. TBTI, KME, HAM license. Lt. (j.g.) USNR. 3 years with missiles and radar. Release from active duty Feb. 1, 1959. Desires position where graduate work may be done, double option, communications and industrial electronics analog computers. Box 1075 W.

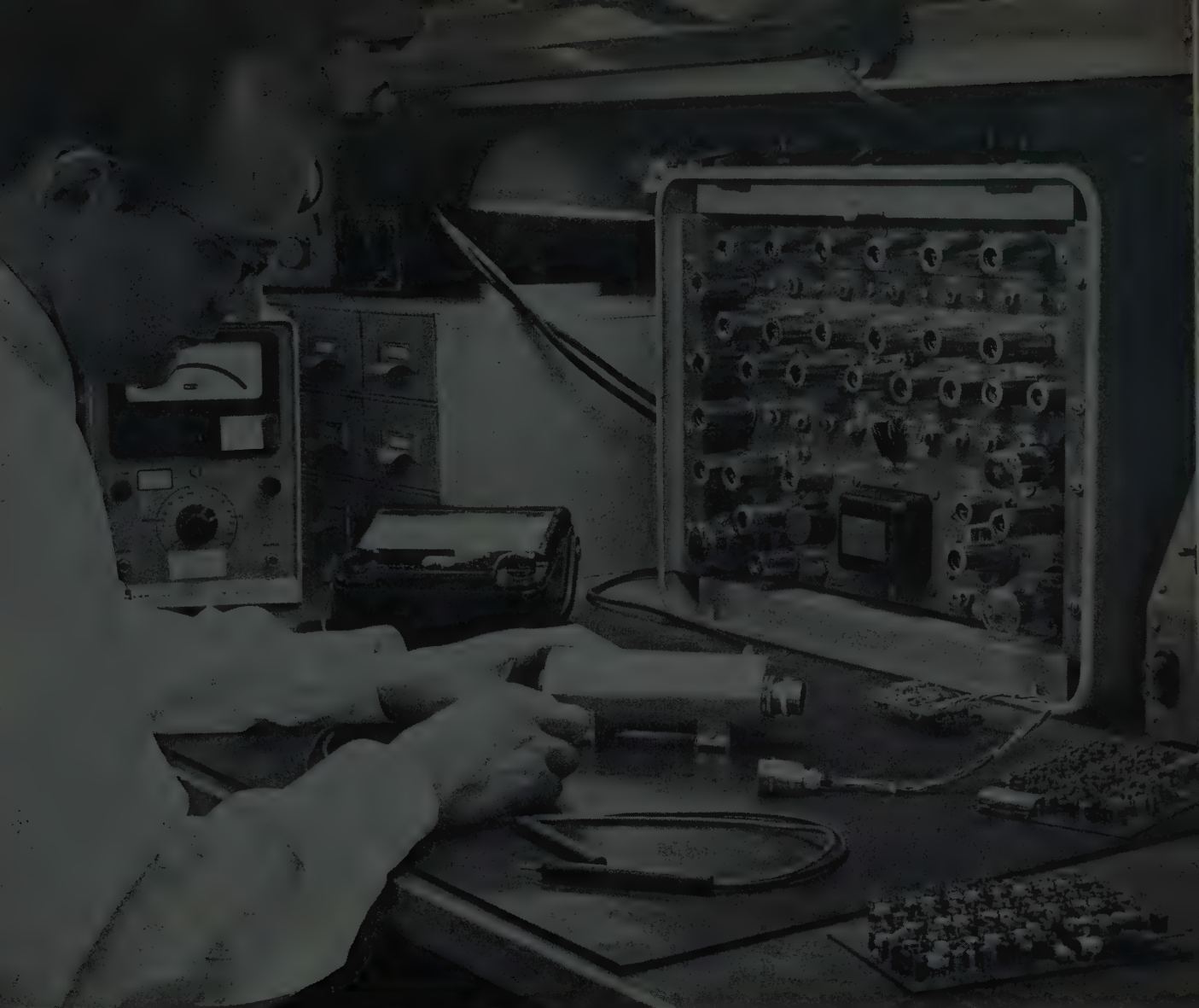
TECHNICAL WRITER

Submarine veteran with college background in E.E. and journalism. Presently program director and FM engineer for small radio station. Successful free-lance writer. Desires position where ability to creatively translate engineers' notes into English will be used. Age 25; married. Box 1076 W.

TELECOMMUNICATIONS ENGINEER

B.Sc. (Eng.) 1st class honors London University, telecommunications. Age 33. 7 years experience in design and construction of every type of electronic equipment. Recent research on semiconductors. A.M.I.E.E., Member IRE. Several publications on circuits. Available in U. S. later this year. Box 1077 W.

(Continued on page 132A)



A MISSILE AND TELEVISION INDUSTRY FIRST. Lockheed-developed, miniaturized TV cameras, designed for both government and commercial use. Only 6 inches long and 2 1/4 inches in diameter, tiny cameras extend man's vision into the unexplored. Unmanned lunar probes to the far side of the moon; lunar landings; monitoring interiors of manned spacecraft and remote TV coverage of on-the-spot happenings on a scope never before possible are some of the uses foreseen for the cameras.

ELECTRONIC ENGINEERS AND SCIENTISTS

Lockheed Missile Systems Division is systems manager for such major, long-range programs as the Navy Polaris IRBM, Earth Satellite, Army Kingfisher, Air Force X-7 and Q-5 ramjet vehicles, and other important research and development programs.

Responsible positions for high-level, experienced personnel are available in research and development, in our project organizations, and in manufacturing.

Particular areas of interest include microwave, telemetry, radar, guidance, solid state, reliability, data processing, instrumentation, servomechanisms, flight controls, circuit design and systems analysis, test, infrared, and optics.

If you hold a degree and are experienced in one of the above fields, we invite your inquiry. Please write to Research and Development Staff, Dept. 3312, 962 W. El Camino Real, Sunnyvale, California.

Lockheed

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SUNNYVALE, PALO ALTO, VAN NUYS, SANTA CRUZ, SANTA MARIA, CALIFORNIA
CAPE CANAVERAL, FLORIDA • ALAMOGORDO, NEW MEXICO

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Excellent salaries are offered to suit your individual experience and educational background. Benefits include insurance, and retirement programs, plus an unusual vacation policy which allows up to four weeks vacation per year. Tuition free graduate study may be taken at Illinois Institute of Technology, which is also located at Technology Center. In addition generous relocation and interview allowances are provided. Further information concerning these positions may be obtained by sending a resume of your qualifications to:

A. J. Paneral

ARMOUR RESEARCH FOUNDATION

of Illinois Institute of Technology

10 West 35th St.

Chicago 16, Ill.

**CHEMICAL AND PETROLEUM ENGINEERS
ELECTRONIC ENGINEERS
PHYSICISTS
COMPUTER ENGINEERS**

DIGITAL COMPUTERS FOR PROCESS CONTROL

The Thompson-Ramo-Wooldridge Products Company is seeking engineers and scientists to participate in the design and application of digital computer systems for the control of manufacturing processes, especially in the petroleum and chemical industries. Staff members work on a variety of processes, studying various control problems and synthesizing control systems which take into consideration the complex factors governing optimum process operation. Applicants holding advanced degrees in engineering, physics, or chemistry are preferred.

*Those interested are invited to write to the
Director of Engineering,*

THE THOMPSON-RAMO-WOOLDRIDGE PRODUCTS COMPANY

POST OFFICE BOX 45067, AIRPORT STATION, LOS ANGELES 45, CALIFORNIA



**Positions
Wanted**



By Armed Forces Veterans

(Continued from page 130)

SENIOR ELECTRONIC TECHNICIAN

Experienced Senior Electronic Technician. Presently Chief Technician. 13 years electronics background; amateur license; 3 years as Radar Theory Instructor; data handling background; digital techniques; magnetic perforated tape handlers. Leadership abilities in supervisory capacities proven by minimum of last 5 years. Desires challenge with opportunity. Box 1078 W.

ENGINEER-PILOT

B.S.E.E., Princeton University. Age 31, married, 2 children. Desires position combining engineering talents and Beechcraft Pilot qualifications in engineering administration, application, liaison, sales or project supervision. 7 years diversified experience encompassing project engineering, flight test and instrumentation, electro-mechanical and electro-hydraulic design, application and sales engineering. Present responsibilities include hydraulics, radar drives and control systems, antenna selection and RF feed assemblies. Considerable experience in cost estimating and preparation of technical proposals. Prefer New Jersey or other eastern location. Box 1079 W.

ELECTRONIC TECHNICIAN

Graduate RCA Institutes. Varied background in machine accounting. Currently maintaining large digital computer airlines reservation system. Audio and industrial electronics interest. Evening E.E. student. Hold 1st class radio-telephone license. Box 1081 W.

MANAGER-ENGINEER

Manager of Electronic or communication engineers—Mature responsible executive; substantial electronic-communication background; fully developed qualities of leadership, resourcefulness and judgement. Able to inspire teamwork and high morale; outstanding achievements in organization, coordination and development of personnel. Box 1082 W.

APPLICATION AND LIAISON ENGINEER

Reserve Signal Officer formerly with combat developments office, U. S. Army Special Warfare School, desires position as application and liaison engineer with company interested in the development of special communications and electronic equipment for military application. Box 1086 W.

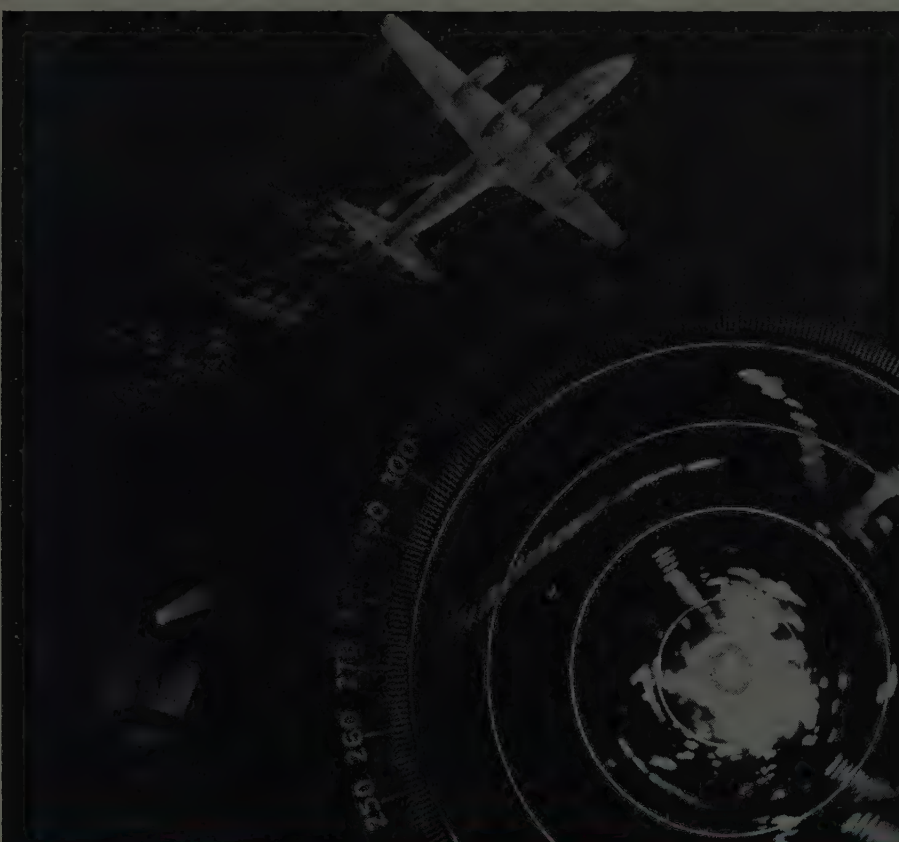
EDUCATOR-AUTHOR-ENGINEER

M.S. School administrator, proven record in course development electronics technology at Community College and technical institute level, desires administrative or training position in school or in electronics or allied industry. Age 47, married, 1 child. Box 1087 W.

ELECTRONIC ENGINEER

Graduated RPI, BEE. 1955. 2 years project and field engineering of lt.wt radar. 1/Lt. USAF with 2 years experience in ECM and large scale digital computer programming. Release from active duty Jan. 31, 1959. Desires project engineering work in the eastern U. S., preferably New York area. Age 24, married. Box 1088 W.

Recent Raytheon achievement in Radar



MOVING-TARGET INDICATOR

is just one of the many dramatic achievements Raytheon engineers are making in radar every day. This development applies the electronic memory of a recording storage tube to a standard plan-position indicator (PPI).

ADVANTAGES: (1) trail of the moving target is displayed on the scope to permit immediate analysis of target course without the necessity of manual plotting. (2) Scope brightness is uniform and at a sufficient level for lighted area viewing!

HOW IT WORKS: both live and stored data are shown on a two-layer, two-color phosphor CRT on a time-shared basis—the stored pattern being read out onto the scope in the time between successive PPI sweeps. A yellow dot indicates the target and a blue-white trail depicts the history of its motion.

To the man who is looking for **FRONTIER PROJECTS IN ELECTRONICS:**

As an engineer or scientist who wants to accomplish more in 1958, you naturally want to be where new things are happening.

Whatever your specialized background and interests, chances are you'll find a current Raytheon project that offers exceptional opportunity for you to put your scientific skill and creative imagination to work.

Raytheon's constant expansion during 1958 covers advanced activities in:

COMMUNICATIONS (Commercial and Military) — scatter, microwave relay, multiplex, mobile transistorized equipment.

COUNTERMEASURES—radar countermeasures equipment, advanced study projects.

RADAR (Pulse and CW Systems)—search, fire control, bombing, navigation, and guidance, air-traffic control, weather and marine, military and commercial.

MARINE EQUIPMENT—submarine, ship and air-borne sonar, depth sounders, direction finders, radars.

GUIDED MISSILES—prime contracts:

Navy Sparrow III (air-to-air)

Army Hawk (ground-to-air)

MICROWAVE TUBES—"Amplitrans," magnetrons, klystrons, traveling wave tubes, storage tubes, backward wave devices.

SEMICONDUCTORS—devices, materials and techniques; silicon and germanium.

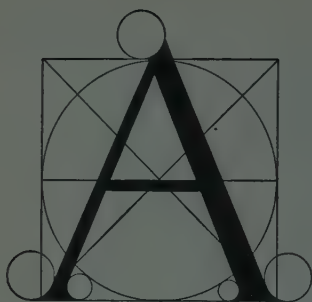
For interview at your convenience, please write to:

E. H. Herlin, Professional Personnel Section
P.O. Box 237, Brighton Station, Boston 35, Mass.

Excellence in Electronics



RAYTHEON MANUFACTURING COMPANY



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holders of advanced degrees
in physics, mathematics,
electrical
and mechanical engineering**

Litton Industries offers research appointments of the highest order of importance to the nation's defense and economic endeavors. Applicants must have proven capability at the professional level for contributions toward the advancement of knowledge in the fields of computation, guidance, communication, or control.

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The locale is Southern California where both the physical and intellectual climates are to be enjoyed. Send a brief resume to G. K. Dawson, Litton Industries, Electronic Equipments Division, 9261 West 3rd Street, Beverly Hills, California.



LITTON INDUSTRIES
Electronic Equipments Division



**Positions
Open**



The following positions of interest to IRE members have been reported as open. Apply in writing, addressing reply to company mentioned or to Box No.

The Institute reserves the right to refuse any announcement without giving a reason for the refusal.

Proceedings of the IRE
1 East 79th St., New York 21, N.Y.

SENIOR ELECTRONIC ENGINEERS

Experienced engineers to design and develop components and systems. Advanced degrees preferred. Positions are with the Seminole Division of Airpax Products Company. Products are of the highest quality; management is young and aggressive; engineering is thoughtful and advanced. The division occupies a new building in Fort Lauderdale, Florida, with ideal living conditions. If you can make a positive contribution to this type of company, and wish to live and work in this kind of atmosphere, send resume to Personnel Director, The Airpax Products Co., P.O. Box 8488, Fort Lauderdale, Florida.

ELECTRONIC ENGINEER

For design and development work with high energy accelerators used in nuclear physics research program. Includes power electronics, pulsed circuits, vacuum systems and magnetic design. Qualifications: degree in electrical engineering or engineering physics, 2 to 5 years experience. Months' vacation, good conditions and benefits, competitive salary. Send resume of personal history, education, experience and reference to Mr. J. J. Cochrane, Physics Research Lab., University of Illinois, Champaign, Illinois.

RECEIVER-AMPLIFIER DESIGN ENGINEER

Engineering experience in the design and packaging of RF and IF amplifiers, VHF and UHF receivers (tube and transistor) desirable but not essential. Company now in its fifth year of operation and is located in the heart of the San Francisco Bay area. Competitive salary and company participation benefits. Send resume to R. S. Electronics Corp., 435 Portage Ave., Palo Alto, Calif.

INSTRUMENTATION ENGINEER

Opening for a graduate engineer with 5 to 10 years experience in commercial design of circuits for instrumentation use. Masters degree preferred. Experience should include pulse circuit, video amplifier and D-C amplifier designs. Specialists in any of these considered. Eastern location. In reply, please state education, experience, age and salary requirements. All replies in strict confidence. Box 1082.

TECHNICIAN

Technician as assistant in electronics services shop maintained in connection with University of Arkansas research program. Salary in the range of \$3600 for 12 months with 2 weeks vacation. Address application or inquiry to Virgil W. Adkisson, Dean, Graduate School, University of Arkansas, Fayetteville, Arkansas.

(Continued on page 136A)



men create at **Magnavox**

Engineers and scientists who thrive on a real challenge...are creative...and interested in unequalled opportunities are cut out for Magnavox. Magnavox...the leader in electronics offers senior-level positions to men of this calibre in the fields of Airborne Radar, ASW, Communications, Navigation Equipment, and Digital Data Systems. Address your inquiries to:

Mr. R. F. Eary, Technical Staffing Director
The Magnavox Company
2131 Bueter Road
Fort Wayne 4, Indiana



R&D ADVANCED ELECTRON DEVICES SOLID STATE COMPONENTS & NETWORKS

Three Positions Of Singular Interest To Physicists And Electronic Engineers

General Electric's Electronics Laboratory—an organization conducting applied research and advance development in every branch of electronics—has openings for men qualified for the following individual responsibilities.

1. To carry out experimental studies on electron optics for special devices such as infrared cameras and/or develop electron-solid-state devices utilizing electron beams interacting with electromagnetic fields.

2. To conduct experimental studies related to masers, parametric amplifiers, infrared detectors, thermoelectric-thermionic power sources, and other advanced electron devices.

3. To assume responsibility for analytical design of, and applied research in magnetic and dielectric solid state devices, sonic transducers, and filters with LC networks.

The professional environment here is one of vigorous intellectual interaction between colleagues working in diverse areas of electronic research and development. More than 70% of the Professional Staff have advanced degrees.

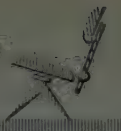
Requirements for all three positions:
Ph.D. in Applied Physics or Electronics (EE) or MS plus three years' applicable professional experience.

Please write to:
Mr. Robert F. Mason,
Div. 48-MX
Electronics Laboratory
Located at Electronics Park

GENERAL ELECTRIC
Syracuse, New York



Positions Open



(Continued from page 134A)

ELECTRONIC CIRCUIT DESIGN ENGINEERS

Electronic Circuit Design Engineers—Several years experience and graduate training desirable (but not required) for challenging circuit design problems. Ability to work in small, outstanding group on varied high caliber design projects e.g. computer techniques application, data accumulation and reduction, pulse amplifier and discriminator design. Phillips Petroleum Company, Atomic Energy Div., P.O. Box 1259-C.T., Idaho Falls, Idaho.

SERVO ENGINEER

Servo Engineer to conceive and analyze complex control systems, analyze and design servo circuitry make functional servo design; determine stabilization measures; assist in bid and proposal preparation. Experience in fire control or missile guidance field desirable. Salaries \$10,000-\$11,000. Write Emerson Mfg. Co., 8100 W. Florissant St., St. Louis 21, Missouri.

INSTRUMENTATION SALES

Man experienced or qualified in the sale of instruments used in the electronic industry. For qualifying person, proven through performance, this will lead to management of this division with partner-like participation. Instruments include "Q" indicators, megometers, bridges, voltmeters, decades, null detectors, counters, mag

(Continued on page 138A)

COLLEGE OF ENGINEERING, UNIVERSITY OF ARIZONA

has opportunities for exceptional
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ADVANCED CELESTIAL NAVIGATION SYSTEMS

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S.E.P.D. was created to apply IBM's wealth of systems knowledge to the development of special-purpose precision equipment related to, but outside of, IBM's regular line of products. Immediately required are creative engineers and scientists — men who enjoy the challenge of working independently on a wide variety of unique assignments.

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Advanced component design
Analog or digital computers
Automation
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Industrial controls
Instrumentation
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Servo systems
Solid-state devices and applications
Telemetry

QUALIFICATIONS:

B.S., M.S., or Ph.D. degree in E.E., M.E., Physics, or Mathematics. Industrial experience desirable.

At S.E.P.D., you will find all the ground-floor opportunities of a new company. You will work on small teams where individual merit is quickly recognized. Assignments are varied and far from routine, and you will have IBM's experienced specialists and technicians for support. In addition, you will enjoy all the advantages of IBM employment, including job stability, liberal company benefits, and excellent salaries.

WRITE, outlining qualifications and experience, to:

Mr. T. P. Bianco, Dept. 645Z
IBM Special Engineering Products Div.
North Hamilton Street
Poughkeepsie, N. Y.



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More than 8 OUT OF 10 ENGINEERS say "yes" to an invitation to join Norden Laboratories



The ratio of 8.3 acceptances for every 10 engineers invited to join Norden Laboratories' professional staff is unusually high, especially in the opportunity-rich electronics industry. We went right to the source and checked new members of our engineering groups, who revealed these factors impelling their decision in favor of Norden:

- Pioneering Nature of the Work in Diversified Electronic Areas
- Small R & D Groups Fostering Individual Accomplishment
- Close Contact With Management
- Flexibility of Assignments
- 30-Year Company History of Achievement in Precision Electronics

If this partial description of the professional environment at Norden Laboratories appeals to you, look into these immediate openings on a variety of advanced projects at both White Plains, New York and Stamford, Connecticut locations:

TELEVISION & PASSIVE DETECTION • TV Display Circuitry
• TV Camera Circuit Design • TV Transistor Circuitry

Also openings for recent EE grads

RADAR & COMMUNICATIONS Design & Development openings in the following areas: Antennas • Microwave Systems • Microwave Components • Receivers • Transmitter Modulators • Displays • Pulse Circuitry (VT & Transistors) • AMTI • Data Transmission • ECM

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STABILIZATION & NAVIGATION • Stabilization Servos

• Amplifiers & Electronics

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• **SR ENGINEER** — Cost development for R&D proposals. Require broad technical experience in electromechanical & electronic systems

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• *Descriptive Brochure Available Upon Request*

After-hour interviews arranged at your convenience.

Send resume in confidence to: **TECHNICAL EMPLOYMENT MANAGER**

NORDEN LABORATORIES

NORDEN DIVISION — UNITED AIRCRAFT CORP.

121 Westmoreland Avenue • White Plains, New York

White Plains, New York

Stamford, Connecticut



Positions Open



(Continued from page 136A)

amps and others. All New England territory. Compensation by commission, with potential exceeding usual "utopian" set-ups. Write to Henry P. Segel, c/o Henry P. Segel Co. Inc., 386 Washington St., Brookline 46, Mass.

ELECTRONIC ENGINEERS

Attractive opportunity with newly formed group in large electronics research center. Involves application of novel techniques, circuits and components to television and radio receivers. Requires B.S. or advanced degree in E.E. with several years experience in receiver development or design. Send resume to Mr. Paul J. Cuomo, RCA Laboratories, Princeton, New Jersey.

ELECTRICAL ENGINEERING DEPARTMENT HEAD

Excellent opportunity available for young teacher with Ph.D. Should have teaching and industrial experience. College located in San Francisco Bay area electronics industry research, development and manufacturing center. Academic rank and salary open. Write to N. O. Gunderson, Head, Div. of Engineering, San Jose State College, San Jose 14, Calif.

ENGINEERS-PHYSICISTS

A limited number of positions are open on the research and development staff of Paul Rosenberg Associates for electronic engineers and physicists of senior and junior grades, to conduct applied research and development. Unusually interesting and challenging R&D in advanced data processing systems and circuitry. Excellent working conditions. Salaries at high industrial levels, commensurate with experience and ability. U. S. citizens only. Applications kept in strict confidence. Send resume and salary desired to Code 12, Paul Rosenberg Associates, 100 Stevens Ave., Mt. Vernon, N.Y.

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E.E.'s and M.E.'s experienced in advanced VHF-UHF systems, test equipment, TV and transistor circuitry, electronic packaging. Permanent; growth opportunities in expanding company. Relocation allowance. Ideal working and living conditions. 35 minutes from New York City. Send resume in confidence to Adler Electronics, Inc., New Rochelle, New York.

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Design and development engineer for antenna and transmission line components with particular emphasis on microwave frequencies. Excellent opportunity to grow with one of the leading antenna manufacturing concerns. Salary commensurate with ability. In an executive status this position also includes a profit sharing bonus. Phone or write Mr. R. T. Leitner, Vice Pres., Director of Engineering, Technical Appliance Corp., Sherburne, N.Y.

PROFESSORS

Professors, Ph.D.; Fields and computers especially. Large graduate program. Income \$9,000-\$12,000 with research. Box 1083.

(Continued on page 140A)



"SPACE CHESS," a painting by Simpson-Middleman, a doubly-gifted team of artists with a scientist's penetrating insight. They portray here "a chess-like game played in a segment of space on a skewed board with pieces of uncertain value against an unknown antagonist. The next move is unforeseen—it will come out of the dark—it will be history's most fateful gambit."

Space-age openings at Boeing

Advanced projects under contract at Boeing include Minuteman, a solid-propellant intercontinental ballistic missile, and Bomarc, America's longest-range area-defense supersonic guided missile system. Also underway at Boeing are studies for orbital, lunar and interplanetary systems.

These programs, along with extensive advanced research efforts at the frontiers of science, have created some of the nation's truly outstanding career opportunities for engineers and scientists.

There are openings at Boeing, now, in research, design, manufacturing and development, in such advanced areas as celestial mechanics, glide vehicles, space trajectories, high speed drag and heating effects

in space flight and re-entry, anti-submarine warfare techniques, gas dynamics, nuclear physics, solid-propellant rocket engines, infrared techniques, anti-missile missiles, advanced electronics, and ion and plasma production and manipulation.

Boeing's space-age orientation, exemplified by advanced studies now underway in ballistic, orbital, lunar, interplanetary and advanced defense systems, has already laid a foundation for continuing leadership in the future. Engineers and scientists of all categories find at Boeing the kind of forward-striding environment that means dynamic career growth. Drop a note now to Mr. Stanley M. Little, Dept. G-83, Boeing Airplane Company, Seattle 24, Washington.

BOEING



Positions Open



(Continued from page 138A)

INSTRUCTORS AND RESEARCH ENGINEERS

Instructors and Research Engineers to work for D.Sc. at University of New Mexico. Large graduate program assures variety of available courses. Write Chairman E. E. Dept. University of New Mexico, Albuquerque, New Mexico.

TEACHERS

Teachers needed for permanent staff in expanding department. Salaries depending on experience and academic background. Write to Electrical Engineering Dept., Louisiana State University, Baton Rouge, Louisiana.

ENGINEERS

The Civil Aeronautics Administration's Technical Development Center in Indianapolis, Ind., is interested in receiving applications from qualified Electronic and Electrical Engineers. The Center is engaged in developing new and improved electronic and electrical aids to the nationwide air navigation and traffic control systems. Vacancies range from \$4490 to \$8810 annually, salary commensurate with years of education and experience. Address inquiries or send resume to Personnel Officer, CAA Technical Development Center, P.O. Box 5767, Indianapolis, Ind.

ELECTRONIC ENGINEERS

The Civil Aeronautics Administration has career positions with excellent promotional opportunity for graduate Electronic Engineers, involving installation and maintenance of electronic air navigational aid equipment. Most positions involve 85% travel over 15 north-eastern states with headquarters at Jamaica, N.Y. Employment is effected in accordance with Federal Civil Service regulations. Grade levels available are: GS-5 \$4490 6 mos. trainee position, GS-7 \$5430, GS-9 \$6285. All travel positions subject to \$12.00 per diem travel allowance. Send application of Standard Form 57 available from Personnel Div. Dept. 91C, CAA, Federal Bldg., International Airport, Jamaica, N. Y.

SCIENCE AND ENGINEERING

Opportunities at Robert College, Istanbul, Turkey for qualified men in engineering, mathematics, physics and chemistry interested in combining teaching and consulting with the opportunity to live and travel in a vital part of the world. Development program is in effect to strengthen staff, modernize undergraduate curricula, inaugurate graduate program, construct new science and engineering building, prepare engineers for the industrial and technological development of Turkey and the Middle East. Address inquiries to Dr. Duncan S. Ballantine, Pres., or Dean Howard P. Hall, College of Engineering, Robert College, Bebek P.K. 8, Istanbul, Turkey, with copy to Near East College Assoc., 40 Worth St., New York 13, N.Y.

PHYSICIST

Magnetics: Theoretical physicist with M.S. or Ph.D. degree and experience in magnetics. Position involves aid to both ceramic and electrodeposition groups, developing new magnetic materials and applications. Send complete resume to K. B. Ross, National Cash Register Co., Dayton 9, Ohio.

(Continued on page 142A)

TUBE ENGINEERS

NEW FLORIDA ELECTRONIC TUBE PLANT OF SPERRY ELECTRONIC TUBE DIVISION

UNUSUAL OPPORTUNITIES ON NEW PROJECTS In The Microwave Tube Field for RESEARCH, DEVELOPMENT and PRODUCTION ENGINEERS

B.S., M.S., or Ph.D's or equivalent, with previous experience or training on magnetrons, klystrons, and traveling wave tubes, etc.

Here you will find a unique, perfect combination for maximum professional development, expression and recognition...a new division, recently started production, offering exceptional growth potential...yet possessing the stability and "Know How" of Sperry's 50 year history of engineering accomplishments.

ENJOY PLEASANT FAMILY LIVING IN FLORIDA

Our plant is located in the University City of Gainesville, Florida, noted for excellent all year round climate, unexcelled fishing, boating and swimming at nearby lake and gulf beaches, uncrowded living conditions with excellent housing available.

PLEASE SUBMIT RESUME TO
EMPLOYMENT DEPT.

SPERRY

ELECTRONIC TUBE DIVISION
of Sperry Rand Corp.
Gainesville, Florida

ELECTRO- MECHANICAL ELECTRONIC ENGINEERS

A BS or advanced degrees in EE, ME, or Physics, may qualify you for a career at NAA, home of the advanced B-70, F-108, and X-15.

Flight Control Analysis, Reliability Analysis, Flight Simulation, Systems Analysis.

Electrical Systems Analysis and Design, Mission and Traffic Control, Fire Control, Bombing Systems, Electronics Systems Integration, Flight Controls, Ground Support Equipment, Airborne and Electronic Test Equipment.

Applied Research in Radome Development, Antenna Development, Infrared, and Acoustics.

Please write to: Mr. B. M. Stevenson, Engineering Personnel, North American Aviation, Los Angeles 45, California.

THE LOS ANGELES DIVISION OF

NORTH AMERICAN AVIATION, INC.



You, too, can PIONEER on such new frontiers

AT TEXAS INSTRUMENTS, you can apply your Master or Doctorate specialty under conditions of substantial freedom. Explore scientific horizons with outstanding associates... using facilities that permit work of highest technical caliber. Expand your professional potential in free exchange of ideas... in an atmosphere where you and your work are recognized as vital.

Favorable research climate is a major factor in the swift growth of this 28-year-old company whose sales rate has increased 20-fold over the last decade. Recognition of individual talent and achievement has helped Texas Instruments grow to be one of the 500 largest industrial companies in the country. To pace TI's leadership, the Central Research Laboratory will soon move its expanding scientific community into a new building designed to establish an even finer creative environment.

Avail yourself of this opportunity for self-expression in creative research. In addition, enjoy TI's generous personnel benefits as well as encouragement and assistance in personal development. TI labs are in the city yet away from downtown traffic... within minutes of fine residential areas, cultural activities, churches, highly rated schools and, of course, year-around *outdoor* recreation in the pleasant climate of the Southwest.

BASIC & APPLIED RESEARCH Masters and PhD's interested in these activities, please write **A. E. Prescott**.

In addition to research, there are excellent openings for ME's and EE's, electronics engineers especially, in—**ELECTRONIC & ELECTROMECHANICAL APPARATUS** Radar, sonar, infrared, optics, magnetics, telemetering, communications, computers, transformers. Write **John Pinkston**.

For **SEMICONDUCTOR DEVICES & OTHER COMPONENTS** Transistors, diodes, rectifiers, capacitors, resistors, transistor circuit applications, test equipment, mechanization, write **Harry Laur**.

***LOW TEMPERATURE PHENOMENA.** While commercial applications in this field may be some time away, the potential is so great in TI's areas of interest that we are engaged in a broad, basic approach to the problems involved. This activity is only one of some 20 subjects now under study at Texas Instruments—covering basic and applied research in solid state physics, materials, devices, data systems, and earth sciences; concentrating on semiconductors, electroluminescence, ferromagnetics, magnetic resonance, superconductivity, dielectrics, infrared, geophysics, computers, memories, and transistors plus physico-chemical studies of diffusion, alloying, crystal growth, and crystalline perfection.



TEXAS INSTRUMENTS
INCORPORATED

5000 LEMMON AVENUE DALLAS 5, TEXAS

GROUND

The crucial ground environment for handling, launch and test of our major missile programs is managed at Cape Canaveral by Pan Am. The Guided Missiles Range Division of Pan American World Airways, Inc. has prime responsibility for managing, operating and maintaining the 5000-mile Atlantic Missile Range.

These operations and the division's continuing growth create unique engineering opportunities in the new and vital arts of missile range management, operation, maintenance and test data collection and reduction.

Qualified physicists, mathematicians and electronic and mechanical ground systems engineers should investigate these openings on the ground floor of the space age with Pan Am. Please address a confidential resume to Mr. C. R. Borders, Assistant Division Technical Manager, Pan American World Airways, Inc., Patrick Air Force Base, Cocoa, Florida, Dept. C-1.



GUIDED MISSILES RANGE DIVISION

PATRICK AIR FORCE BASE, FLORIDA

DIGITAL COMPUTERS AND CONTROL SYSTEMS

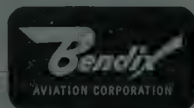
- AIRBORNE DIGITAL EQUIPMENT
- NUMERICAL MACHINE CONTROL
- HYBRID ANALOG-DIGITAL SYSTEMS

Engineers and scientists needed with experience in all phases of digital computer design and development. Systems organization, logical design, transistor circuitry, magnetic core and drum memories, input-output equipment, packaging. Applications include airborne digital equipment, numerical machine control, and hybrid analog-digital systems. Both commercial and military applications emphasizing advanced development and research. We think you will find this work unusually stimulating and satisfying. Comfortable and pleasant surroundings in suburban Detroit.

If interested, please write or wire Fred I. Barry,
Research Laboratories Division, Bendix Aviation Corporation
P. O. Box 5115, Detroit 35, Michigan

Research Laboratories Division

SOUTHFIELD, MICHIGAN



**Positions
Open**



(Continued from page 140A)

TEACHERS

Excellent opportunity is available in a new expanding department. Location is at medium sized university in the midwest devoted primarily to undergraduate teaching. Rank and salary commensurate with qualifications. Appointment is available beginning February or September. Send complete resume to Box 1084.

ELECTRONIC ENGINEER

Electronic Engineer to teach lecture and laboratory courses. Up-to-date knowledge of the field required. Working and living conditions excellent; salary and opportunity very attractive. Write to Dean of Engineering, California State Polytechnic College, San Luis Obispo, Calif.

PROFESSORS

Teaching positions—Assistant, Associate, or full professor of Electrical Engineering, M.S. or Ph.D. required. 9 month salary range presently \$5000-\$9000. Full year appointments available. Salaries are increasing rapidly. Candidate should be well prepared to teach in new undergraduate program with strong engineering science emphasis and in E.E. graduate (M.S.) program. Apply to A. T. Murphy, Head, Dept. of E.E., University of Wichita, Wichita 14, Kansas.

ELECTRONIC AND MICROWAVE ENGINEERS

Minimum requirements: B.S. in E.E. All levels of engineers from junior to project management level. Company is concerned with design of components and instruments for communications, guided missiles, fire control systems and radar systems. Convenience to Polytechnic Institute and graduate study. Tuition half paid. Salary \$6,000 to \$12,000. For inquiries: Thorndike Deland Associates, 1440 Broadway, New York, N.Y.

ELECTRONIC ENGINEERS—PHYSICISTS

Intermediate and senior positions open in long range programs in each of the following projects: satellite, space, electronic test equipment, instrumentation. Opportunity for advance degree, 4 weeks vacation, excellent working conditions. Submit resume and college transcript to Mr. J. Prager, New York University, Research Div., 401 West 205th St., New York 34, N.Y.

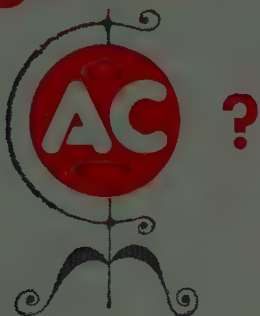
ENGINEERS

Good pay, \$7,856 to \$11,012, with 25% cost of living allowance which is tax free for federal income purposes, work with the most advanced electronic equipment, and the great outdoors, are attractions held out to engineers by the CAA in Alaska where opportunities steadily increase. CAA means travel, adventure, challenge. Civil Aeronautics Administration, Regional Administration, P.O. Box 440, Anchorage, Alaska.

SYSTEMS PROJECT ENGINEER

Manage full program pertaining to research and development of complex airborne navigational systems for application in aircraft, missiles, and space vehicles. Responsible for project administration as well as technical guidance of group. Send resume to Charles J. Weinpel, Kearfott Company, Inc., 1500 Main Ave., Clifton, New Jersey.

How far can an engineer go at



Someday your name may go on the door of a top-management office of the AC Division . . . or of the General Motors Corporation. This is part of GM's "open door" policy. This means that not only is every GM door open to every employee, but that every open door represents opportunity. Today AC helps fulfill the large demand for inertial guidance systems (with the AChiever) and many other electro-mechanical, optical and infra-red devices. In the future AC will supply even more instrumentation needs—both military and commercial—for the "space era." Your long-range prospects at AC can hardly be equaled. You'll gain invaluable experience working shoulder to shoulder with recognized experts on many assignments. You'll enjoy highest professional status, which can be enhanced by working on advanced degrees at engineering schools located near AC facilities. You can work at AC facilities across the country or around the world. In short, if you are a graduate engineer in the electronic, electrical or mechanical fields, *you can go places at AC, because AC is going places.* This is worth looking into. Just write the Director of Scientific and Professional Employment: Mr. Robert Allen, Oak Creek Plant, Dept. E, Box 746, South Milwaukee, Wisconsin; or Mr. M. Levett, Dept. E, 1300 N. Dort Highway, Flint 2, Michigan. It may be the most important letter of your life.

Inertial Guidance Systems • Afterburner Fuel Controls • Bombing Navigational Computers
Gun-Bomb-Rocket Sights • Gyro-Accelerometers
Gyroscopes • Speed Sensitive Switches • Speed Sensors • Torquemeters • Vibacall • Skyphone

AC SPARK PLUG  THE ELECTRONICS DIVISION OF GENERAL MOTORS

The strange shape



of defense

This plastic balloon, resting on a mobile trailer bed like a golf ball on a tee, protects the new Hughes three-dimensional radar antenna.

Frescanar, the exclusive system combining high-speed data processors and a frequency scan radar antenna, has been developed by Hughes engineers in Fullerton, California.

Sensitive to the inadequacies of conventional radar, these Hughes Fullerton engineers have devised a radar antenna whose pointing direction is made sensitive to the frequency of the electromagnetic energy applied to the antenna. This frequency sensitivity results in the radar beam being radiated from the antenna at different angles, depending on the frequency of the energy supplied. With the supply of a succession of frequencies, the antenna beam can be moved through a succession of positions. Utilizing this advanced technique, range, bearing and altitude can be detected... on a single antenna.

This Hughes-developed radar system has been combined with compact, high-speed Hughes data processors to provide a completely self-sufficient, mobile radar defense system.

Other Hughes projects provide similarly stimulating outlets for creative engineering talents. Current areas of Research and Development include Advanced Airborne Electronics Systems, Space Vehicles, Nuclear Electronics, Subsurface Electronics, Ballistic Missiles... and many more. Hughes Products, the commercial activity of Hughes, has assignments for imaginative engineers for research in semiconductor materials and microwave tubes.

The diversity and advanced nature of Hughes projects provides an ideal environment for the engineer or physicist interested in advancing his professional status.

An immediate need now exists for engineers in the following areas:

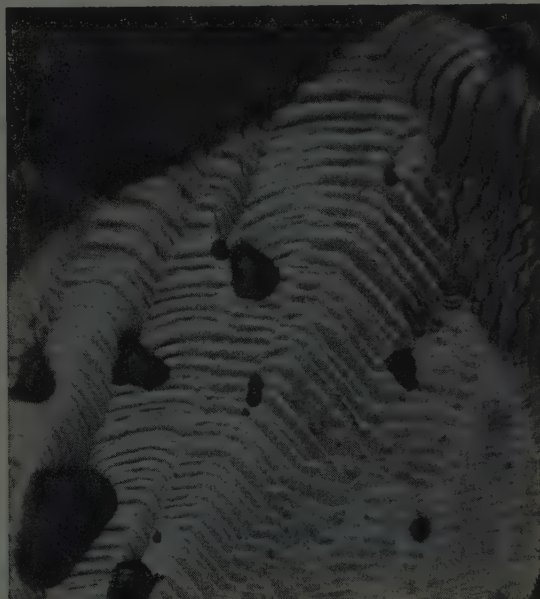
Microwave & Storage Tubes	Reliability Engineering
Field Engineering	Systems Analysis
Quality Control	Circuit Design
Semiconductors	Communications
Digital Computer Engineering	Radar

*Write in confidence, to Mr. Phil N. Scheid,
Hughes General Offices, Bldg. 6-H-2, Culver City, California.*

© 1958, HUGHES AIRCRAFT COMPANY



The Hughes Communications Laboratories have as one objective the development of systems capable of deflecting their signals from meteors, artificial satellites and even the moon.



This photomicrograph of an etched silicon sphere is used in basic studies of semiconductor materials at Hughes Products, the commercial activity of Hughes.

The West's leader in advanced ELECTRONICS

HUGHES

HUGHES AIRCRAFT COMPANY
Culver City, El Segundo,
Fullerton and Los Angeles, California
Tucson, Arizona

THE PERCEPTRON

A RESEARCH TOOL FOR THE STUDY OF PERCEPTION,
MEMORY, AND THINKING BY MACHINES



A NEW FRONTIER

AT CORNELL AERONAUTICAL LABORATORY

Currently under study at C.A.L. is a unique non-biological system capable, without human assistance, of absorbing, identifying, classifying, memorizing and utilizing data to form concepts. Extending the basic theory of the Perceptron and exploring its potentialities is a current C.A.L. research project. We seek to advance and enlarge scientific and engineering knowledge in the area of artificial intelligence. It is a goal that requires imaginative men motivated by an urge to breach barriers. To qualified people, we offer participation in advancing this exciting new field in a climate conducive to personal progress and ready recognition of individual contributions and attainments.

CORNELL AERONAUTICAL LABORATORY, INC. of Cornell University



WRITE FOR FREE REPORT

The story behind Cornell Aeronautical Laboratory and its contributions to aeronautical progress is told in a 68-page report, "A Decade of Research." Whether you

are interested in C.A.L. as a place to work or to watch, you will find "A Decade of Research" both useful and pertinent. Mail the coupon now for your free copy.

J. P. Ruch

CORNELL AERONAUTICAL LABORATORY, INC.

Buffalo 21, New York

Please send me "A Decade of Research."

Name _____

Street _____

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Zone _____

State _____

☐ Please include employment information



These manufacturers have invited PROCEEDINGS readers to write for literature and further technical information. Please mention your IRE affiliation.

(Continued from page 128A)

Tunable UHF Cavity Filter

A new Tunable UHF Cavity Filter has been developed by Adams-Russell Company, Inc., 292 Main St., Cambridge 42, Mass. This cast aluminum cavity is silver plated for low loss and pressure-tight to prevent the entrance of moisture and dust.



The Model 210 covers the frequency range of 200 to 420 mc and has a power rating of 300 watts CW. This filter provides: reduced interference between adjacent transmitter-receivers operating in same location; preselection for receivers with reduced images and other spurious responses; reduced harmonic radiation from transmitters, (40 db typical for second harmonic); and the capability to multiplex several receivers or transmitters into a common antenna.

Specifications include: insertion loss: Approximately 0.5 db; "Q" Factor: Approximately 150; VSWR: 1.3 (in 50 ohm system); 9 1/4 inch diameter X 9 inches high.

Special units are available with narrower passbands and for other frequency ranges. Also available are dual units which comprise two model 310's in cascade. These dual units have a much steeper cut-off characteristic for a given bandwidth. Write for technical data to the company.

Transistor Test Equipment

A new line of transistor tests sets, the KP-2 Series, is now available from Baird-Atomic, Inc., 33 University Rd., Cambridge 38, Mass. The new sets feature extended testing ranges for analyzing transistors at frequencies from 100 cps to 200 kc. They offer ranges up to 2 amperes, 200 volts with two regulated semi-conductor power supplies for bias voltages and currents.

The standard model in the KP-2 Series is rated up to 1 ampere, 100 volts. Other

(Continued on page 148A)

Engineers seeking stimulating careers set a course to Link...in Binghamton, New York

Set sail on a well-charted course! Engineers with a circumspect eye on the future choose their place of employment only after careful, soul-searching deliberation. Link Aviation, Inc., Binghamton, N.Y., has all the necessary ingredients for stimulating careers:

The company—As the pioneer and leading producer of electronic flight simulators, Link has greatly expanded its capabilities in fields such as automatic control, optical and visual display systems and data processing. For example, Link is now the world's largest producer of analog computing equipment.

Working environment—Management men are engineers. They understand your work and point of view. This kind of administration provides engineering thinking right up to policy level.

Living environment—Binghamton, N.Y. is a delightful place to live. Located at the tips of the famous Finger

Lakes, Link-Binghamton abounds in year-round recreation...boating, fishing, hunting, water skiing and camping. Charming homes, modern schools, and convenient shopping centers are in abundance.

Additional benefits—include excellent salaries, generous hospital, health, retirement and profit-sharing benefits, and graduate level courses underwritten by Link.

The positions—Openings at all levels exist for engineers qualified in the following fields: Analog computers, digital computers, radar simulators, automatic checkout equipment, complex electronic simulators, optical systems and electronic packaging.

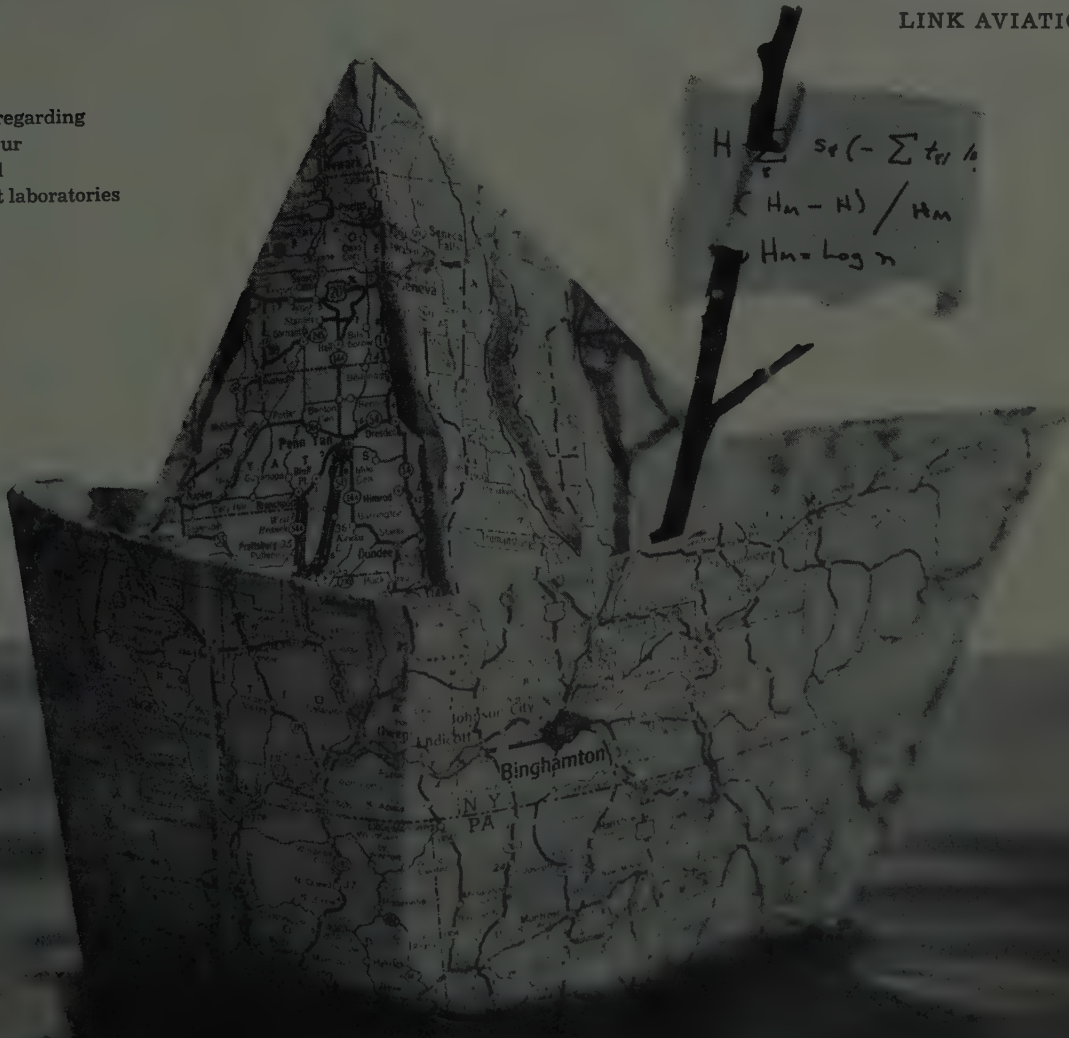
Hoist anchor now! Write to
Mr. W. R. Weiland, Link Aviation, Inc., Binghamton, N.Y.

A subsidiary of
General Precision
Equipment
Corporation



LINK AVIATION, INC.

Write for
information regarding
openings at our
Research and
Development laboratories
in Palo Alto,
California.





The Amherst Laboratory

SYLVANIA'S CENTER FOR COMMUNICATIONS

RESEARCH AND DEVELOPMENT

Sylvania offers to the talented engineer or scientist opportunities for creative research, technical leadership, project responsibility, professional growth.

Unexcelled Promotional Opportunities: Sylvania Amherst is broadening its base in the communications field. Those who will join us now will form the nucleus for the future expansion of the laboratory over the next decade. Promotional opportunities are expected to be unexcelled during the next few years.

At Sylvania you may advance either as a manager or as a scientific specialist, on the basis of your individual contributions. Parallel avenues of advancement are provided with equal rank and salary scales.

Challenging Assignments: Basic investigations having the objective of adding to our store of knowledge in such fields as wave propagation, radio physics, finite group theory, and stochastic processes... applied research designed to advance the state of the communication art through theoretical and experimental investigations in such areas as statistical communication theory, physical characteristics of communication channels, and digital circuit techniques... determination of communication system requirements, application of new discoveries and techniques to specific communication problems, analysis of system characteristics and performance, design and testing of feasibility breadboard models of proposed communication systems... design and fabrication of developmental models of communication equipment.

Professional Development: Employees are encouraged to keep abreast of their fields through regular attendance at meetings and to publish the results of their research in appropriate journals... time off with pay for education courses with up to 100% reimbursement for tuition... 50% reimbursement for professional periodical subscriptions and memberships.

Modern Facilities: Brand new, completely air-conditioned laboratory attractively located in a suburban residential community near Buffalo, Niagara Falls and the Niagara Frontier. Unexcelled opportunities for boating, sailing, swimming and fishing on Lake Erie and Lake Ontario.

Please write: Dr. Robert Malm

AMHERST LABORATORY • SYLVANIA ELECTRONIC SYSTEMS

A Division of

SYLVANIA
SYLVANIA ELECTRIC PRODUCTS INC.

1199 Wehrle Drive, Amherst 21, New York



**NEWS
New Products**



These manufacturers have invited PROCEEDINGS readers to write for literature and further technical information. Please mention your IRE affiliation.

(Continued from page 146A)

models are available up to 2 amperes, 200 volts. All models are available with built-in VTVM and oscillator for an additional \$450 if desired.



Maximum power capacity for the KP-2 Series is 75 watts at present, due to the limitations of transistors now available for the power supplies.

Converter, Recorder and Data Transmission Literature

Milgo Electronic Corp., 7610 N.W. 37 Ave., Miami 47, Fla., has announced four new data sheets.

The Model 1005 Digital Data Transmission System is utilized to transmit and receive digitized Cartesian coordinate and control data.

The Model 3015 provides two simultaneous ink recordings, each consisting of an X-Y or X-H plot in a Cartesian coordinate system.

The Model 3040 coordinate converter will operate as either a Polar to Cartesian or Cartesian to Polar Recorder.

The Model 1500 Cartesian to Polar coordinate converter positions either radars or telescopic photographic recorders.

Filament Heater Power Supply

Two dc power supplies in one is this rugged, compact unit which provides two



(Continued on page 150A)

Sylvania's Expanding Mountain View Laboratories Offer You...

CREATIVE CHALLENGE TO APPLY YOUR ABILITIES TO CONCEPTION AND DEVELOPMENT OF COMPLEX NEW SYSTEMS AND COMPONENTS ADVANCING THE STATE OF THE ART. **ADVANCEMENT** BASED ON INDIVIDUAL CONTRIBUTION WITH FULL AUTHORITY TO EFFECTIVELY CARRY OUT RESPONSIBILITIES. **CALIFORNIA** SUBURBAN LIVING ON THE SAN FRANCISCO BAY PENINSULA.

SYSTEM STUDIES

Analysis & logical design of digital computer circuits. 7 or more years experience desirable in varied phases of electronic systems analysis with emphasis on computer logic. Advanced degrees desirable.

RECONNAISSANCE SYSTEMS LAB

R&D and Fabrication of reconnaissance systems & equipment.

COMPUTERS & DATA HANDLING

D&D of transistorized circuits & high speed digital computer elements. Openings at all levels for engineers with experience in computer design & transistorized circuits.

ELECTRONIC PACKAGING

Packaging of airborne electronic subminiaturized equipment. 7 or more years experience in electro-mechanical packaging of electronic equipment desired.

RELIABILITY

Conduct statistical analysis of complex electronic circuits to determine reliability characteristics of the system. Degree in Statistics desirable with 5 or more years experience in some phases of electronics reliability studies.

DEVELOPMENT ENGINEERING

To perform circuit & equipment design and development in the areas of direction finding, data handling, passive detection, receivers, RF circuits and antennas.

MICROWAVE TUBE LABORATORY

R&D and Production of special purpose microwave tubes.

TUBE ENGINEERS

Design, construction & testing of Traveling Wave tubes. Minimum 1 year experience in test & evaluation of TWT's.

TUBE APPLICATION ENGINEERS

Familiarity with tube specifications & test procedures. To work directly with customers to satisfy their requirements. Requires varied background in electronics & microwave tubes.

SR MECHANICAL ENGINEERS

Perform mechanical design & test of tubes, components & tooling. 5 years experience in mechanical design of vacuum tubes, solenoids & microwave plumbing or developing, testing & evaluating special purpose tubes.

TUBE PRODUCTION ENGINEERS

Construction & manufacture of special purpose microwave tubes. 3-5 years experience in vacuum tube production technique.

MICROWAVE ENGINEERS

Plan & perform microwave experiments on ferrites & gaseous electronic phenomena in relation to development of microwave control devices. Experience in microwave transmission & measurement required with experience in high vacuum systems desirable.

MICROWAVE PHYSICS LAB

Research & advanced development: areas of magnetic ferrites & gaseous electron physics.

RESEARCH SCIENTISTS

To perform theoretical analysis & conduct experiments in production of ultra-violet radiation, microwave breakdown in molecular gases & the transmission of electromagnetic waves through ionized shock fronts & plasmas. Background in electromagnetic theory, plasma physics, gas discharges, & atomic physics desirable, as well as knowledge of microwave measurement techniques & vacuum systems. Advanced degrees desirable.

ELECTRONIC DEFENSE LAB

R&D and Fabrication of electronic countermeasures systems & equipment.

SYSTEMS ENGINEERS

With special interest in advanced systems planning for electronic countermeasures systems, systems analysis, experimental & theoretical susceptibility studies, aerodynamics applied to problems by use of analog computer simulation, applied statistics involving decision, theoretic techniques, laboratory test & integration of electronic systems. Academic work beyond bachelor degree or research experience in experimental physics, statistics or electronics desirable.

FIELD ENGINEERS

To work in field on varied domestic & foreign assignments, to install electronic equipment, perform engineering tests, train military personnel & provide engineering assistance to military commanders. BS degree required plus industrial or military electronics experience.

ELECTRONIC ENGINEERS

Research & advanced development in the fields of electronic countermeasures & electronic systems; particular areas of activity are transmitters, receivers, analyzers, direction finders, data handling, RF circuits & antennas. Experience and/or advanced academic training are especially desirable.

MECHANICAL DESIGN ENGINEERS

Electromechanical design experience, preferably in microwave systems, equipment & packaging. Ability to originate & direct design, to follow through projects. Also engineering experience on high performance precision hydraulic drive & servo control, as in large antenna pedestals. Requires proven creative ability.

Please send your resume to
Mr. J. C. Richards



SYLVANIA

SYLVANIA ELECTRIC PRODUCTS INC.
P.O. Box 188—Mountain View, California

Electronic Engineers

Mechanical Engineers

Physicists

Immediate openings are available in Collins Radio Company's expanding engineering staffs in Cedar Rapids, Dallas and Burbank. You may join one of the closely knit research teams contributing significant advances in the areas of —

- Communication Systems
Single Sideband, Transhorizon, Microwave
- Space and Missile Electronics
- Aircraft Systems
Communication, Navigation, Instrumentation, Control
- Antennas
- High Speed Data Transmission

Opportunities exist in research and development, systems engineering, reliability engineering, field service and sales. Write for more information, or submit complete resume of education and experience to:

G. G. Johnson
Collins Radio Company
855-C 35th Street N.E.
Cedar Rapids, Iowa

J. D. Mitchell
Collins Radio Company
1930-C Hi-Line Drive
Dallas, Texas

F. W. Salyer
Collins Radio Company
2700-C W. Olive Avenue
Burbank, California



CREATIVE LEADER IN ELECTRONICS

NEWS New Products

These manufacturers have invited PROCEEDINGS readers to write for literature and further technical information. Please mention your IRE affiliation.

(Continued from page 148A)

continuously adjustable dc power outputs, 6 to 10 volts, 50 amperes, and 6 to 10 volts, 10 amperes. Power from each output can be drawn separately or simultaneously. The manufacturer claims voltage regulation of ± 0.5 per cent, ripple of 60 millivolts maximum peak to peak, and recovery time of 0.2 second.

Designated type D-10-10-100KS4, this unit was designed by **Christie Electric Corp.**, 3410 W. 67th St., Los Angeles 43, Calif., as part of the ground support equipment for one of the nation's leading missile programs with reliability as an essential requirement. Rugged construction coupled with hermetically sealed silicon diode rectifier elements enable this unit to meet specification MIL-E-4970.

For more detailed information on this unit or other militarized dc power supplies write to Christie.

New Semiconductor Devices

Several new semiconductor devices developed at **Bell Telephone Laboratories**, 463 West St., New York 14, N. Y., were described at the Annual Meeting of the IRE Professional Group on Electron Devices

which was held in October in Washington, D. C. Included were a diffused silicon diode, a high current silicon switching transistor, and a family of high frequency diffused germanium transistors.



T. J. Vasko of Bell Telephone Laboratories is diffusing recombination centers into a slice of silicon to control the reverse recovery time for the completed diodes.

A new diffused silicon diode designed for moderately high speeds and high forward currents was described in a paper prepared by Messrs. P. Zuk, E. Lampi, and J. B. Singleton of Bell Laboratories. This diode exhibits a recovery time as short as 0.02 microsecond. Typical forward voltage drop is 0.75 volt at 100 ma. Ampere currents may be handled on a pulse basis in a miniature package and steady state ampere currents in larger units. The diode is particularly useful for switching applications, including magnetic core circuitry. Zero bias capacitance is less than 25 μf , breakdown greater than 100 volts, and

(Continued on page 152A)



Opportunities in Solid State Electronics

Pacific Semiconductors, Inc., a subsidiary of the Thompson-Ramo-Wooldridge Corporation, has several excellent Technical Staff opportunities as a result of the rapid expansion of its development programs on Very High Frequency and Very High Power Silicon transistors. We invite inquiries from Solid State Physicists and Engineers with experience in transistor development; mechanical engineers engaged in transistor package and manufacturing equipment development; and electrical engineers experienced in semiconductor device applications and test equipment development.

If you have a B.S., M.S., or Ph.D. degree in physics or engineering, applicable experience, and are interested in the future of semiconductor electronics with a young, dynamic organization where resourcefulness and original thinking are both recognized and encouraged, write:

Technical Staff Employment

Pacific Semiconductors, Inc.

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Senior Circuit Designers—Experienced in the design, development and analysis of transistorized computer circuits. Familiar with the application of magnetic cores to computer high-speed memory design. Growth opportunities involving decision making, concerning reliability, cost and component selection are offered. Advanced degree desired.

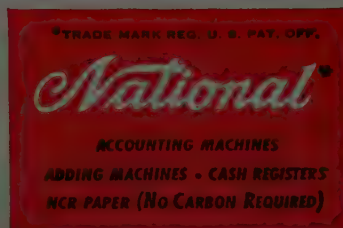
Senior Circuit and Logical Designers—Similar experience and duties as noted for Senior Circuit Designer, plus evaluation and de-bugging arithmetic and control areas of computer systems. Advanced degree desired.

DATA PROCESSING ENGINEERS

Senior Electronic Design Engineers—Experienced in development of logical design using standard computer elements, must also evaluate and design transistorized circuits including voltage regulated power supplies and circuitry related to decimal to binary coding. This data processing system is concerned with bank automation.

SEND RÉSUMÉ TO:

Mr. K. L. Ross
Professional Personnel Section J,
The National Cash Register Co.
Dayton 9, Ohio



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(Continued from page 150A)

saturation current at 40 volts is less than 0.1 microampere at 25°C.

Solid state diffusion techniques are employed to form the junction and to provide the proper recombination center distribution to control the reverse recovery time characteristic. The wafers are sealed in a vacuum tight can and baked at 300°C or higher in a high vacuum to insure stability.

Switching Transistor

A switching transistor developed for high current, high speed applications such as switching magnetic memories was discussed in a paper prepared by C. A. Bittman, J. F. Aschner, J. J. Kleimack, W. F. J. Hare and N. J. Chaplin. This is an *n-p-n* silicon unit with a diffused base and diffused emitter.

The transistor is designed to operate as a switch at the $\frac{1}{2}$ ampere level. At this level, the large signal current gain is 20 and saturation voltage drop 4 volts. The rise, storage and fall times are each of the order of 0.1 microsecond, and the alpha cut-off frequency is greater than 50 mc.

High Frequency Diffused Transistors

N. C. Vanderwal discussed the design and development of small diffused germanium transistors as millimicrosecond switches and 100-500 mc oscillators and amplifiers. Objectives of the development program are transistors having high gain at high frequencies, reliability, low cost, and small size.

Vanderwal reported on some of the workable fabrication techniques, such as collector bonding and encapsulation designs, which have shown promise. He also presented some reliability evaluation results.

New Type Radar Antenna

A new radar antenna that may be the forerunner of antennas for powerful, long-range, antimissile radars of the future has been announced by the Westinghouse Electric Corp., Box 2278, Pittsburgh 30, Pa. An important characteristic of the antenna—known as a Helisphere—is that it scans the sky throughout a complete circle without any motion of the antenna structure itself. In contrast, a conventional radar antenna must rotate continually as it sweeps the sky in search of flying aircraft. In addition, the Helisphere antenna is extremely effective in concentrating high-frequency radar waves into an intense, narrow, moving beam.

"The Helisphere radar antenna has several advantages over conventional types," Dr. John Coltman said. "A non-rotating design permits faster scan and track rates and eliminates the driving power normally required to turn it. An-

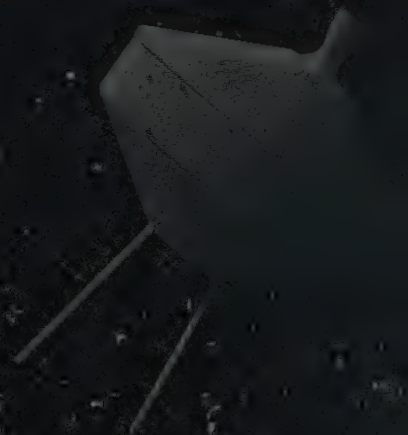
(Continued on page 154A)

the Pioneer in space

To send the U.S. Pioneer more than 60,000 miles into interplanetary space, Space Technology Laboratories in seven months designed, developed, assembled, and tested an 88-foot combination of three integrated stages with a payload incorporating 36 separate ignition systems. STL's Astrovehicles Laboratory focused on the payload itself and the sensitively related problems of propulsion, weight, and stability. These are in addition to the overall complexities of the structural configuration.

Pioneer, setting new apogees in science and missilery, typifies the achievements STL is making in the advancement of space technology. Those who are able to contribute to and benefit from these developments are invited to consider joining our staff.

Space Technology Laboratories



Space Technology Laboratories, Inc.
5730 Arbor Vitae Street, Los Angeles 45, California

WEAPONS SYSTEMS SCIENTISTS AND ENGINEERS

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ELECTRONIC DESIGN ENGINEER

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Responsible for the development of advanced circuitry required for the application of digital techniques to the navigational art.

Kearfott is ideally located in the metropolitan Northern New Jersey area. Please send confidential inquiries to:

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Engineering Division

KEARFOTT COMPANY, INC.
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**NEWS
New Products**



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(Continued from page 152A)

tenna construction is simplified and the problem of rotating bearings—especially acute in large ground-based radar systems—is done away with. The Helisphere secures these advantages by substituting motion of radar energy inside the antenna for the customary rotation of the antenna structure itself.



Scale model—actual size has 100 foot diameter.

"Experimental versions of the Helisphere have included both rigid and inflated balloon-shaped models," Dr. Coltman said. "The inflated version offers the additional advantage of a large structure that is light in weight, portable, and quickly and easily erected."

The antenna was developed by Eugene Kadak and James M. Flaherty, research engineers at the Westinghouse Research Laboratories.

Essentially, the Helisphere antenna is a sphere, either inflated like a balloon or of rigid construction like a plastic globe. On the surface of the sphere, or imbedded in it, are narrow metal conducting strips. These strips wind around the sphere in an endless spiral shape, or helix, as do the threads on a wood screw. It is from this peculiar helical layout on the sphere that the Helisphere gets its name.

Operation of the Helisphere depends upon the fact that radar waves can be polarized, that is, made to vibrate back and forth in a single plane. These polarized radar waves are sprayed against the inside surface of the sphere in such a manner that they vibrate parallel to the thin conducting strips on the sphere. When so oriented, the surface acts as a reflector for the radar waves and reverses their direction back to the other side of the sphere.

Because of the nature of a helix, the strips on the opposite surface of the sphere lie at right angles, not parallel, to the reflected radar waves. Therefore, the waves pass through these strips without reflection and continue on into space as a narrow radar beam.

(Continued on page 156A)

Assignment in GERMANY for SEMICONDUCTOR ENGINEERS

GERMANY—One year assignment at our GERMAN semiconductor division for engineers with proven ability to develop high frequency transistors. (If married, transportation expenses will be paid for family also.) Position guaranteed in our Waltham, Mass. semiconductor operation after completion of assignment in GERMANY.

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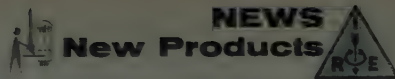
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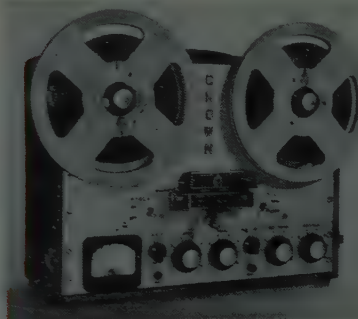


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(Continued from page 154A)

Stereo Recorder

International Radio & Electronics Corp., South 17 St. & Mishanka Rd., Elkhart, Indiana, is now marketing the new Gold Crown Prince Stereo which records and plays a half-track monaural and plays stereo to two cathode follower outputs. Frequency response: 30-30,000 cps ± 2 db at 15 ips; 20-20,000 cps ± 2 db at $7\frac{1}{2}$ ips; 30-10,000 cps ± 2 db at $3\frac{3}{4}$ ips. Flutter and wow: 0.07 per cent at 15 ips; 0.09 per cent



at $7\frac{1}{2}$ ips; 0.20 per cent at $3\frac{3}{4}$ ips. This instrument has a silver satin anodized aluminum finish, magnetic brakes, magnetic

payoff and magnetic takeup, fast forward and fast reverse, 3 motor, 3 speeds, $10\frac{1}{2}$ inch reels with regular transport, (with long play transport up to 14 inch reels), 2 input channels, 2 microphone preamplifiers, and crown "Micro-Mil" heads.

Semi-Conductor Directory

Allied Radio Corp., 100 N. Western Ave., Chicago 80, Ill., announces the publication of a Semi-Conductor Directory, available free on request to all transistor and diode users.

The directory covers about 1000 transistors and diodes available from Allied's stocks at OEM prices, and produced by 13 major manufacturers (Amperex, General Electric, Hoffman Electronics, Hughes Aircraft, International Rectifier, International Resistance, Motorola, Pacific Semiconductors, Philco, Raytheon, Radio Corp. of America, Sylvania, Texas Instruments).

Each transistor, diode and rectifier is listed by part number, name of manufacturer and OEM price in quantities up to 1000 pieces. The directory is constantly being revised and is issued several times each year.

Requests to be placed on the mailing list may be sent on company letterheads to the firm.

Microwave Test Equipment

A line of electronic test equipment for the measurement of impedance, attenuation, and other microwave properties with-

(Continued on page 158A)

ELECTRONICS MANAGER FOR RESEARCH DIVISION Curtiss-Wright Corporation

An outstanding opportunity for an executive scientist to assume complete technical and administrative responsibility for the electronics and ultrasonics research of this new facility located in Quehanna, Pennsylvania (40 miles north of State College — Pennsylvania State University).

This department is currently engaged in research and development relating to aircraft and industrial instrumentation, air traffic control and computer devices. This technical executive will be expected to expand current research programs as well as initiate new research in the fields of commercial and military electronics. Salary is open and there are excellent liberal executive benefits.

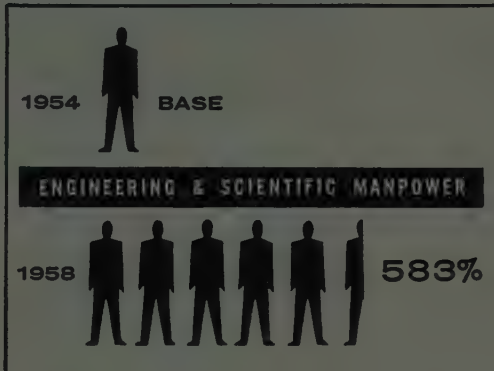
Complete and detailed resume should be sent to: T. W. Cozine, Mgr., Executive & Technical Placement, Curtiss-Wright Corporation, Dept. RD-55, Wood-Ridge, N. J.

All resumes and contacts will be held in complete confidence.

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To consult on semi-conductor problems. Requires knowledge of application of solid state devices in electronics engineering; theory of semiconductors etc.

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1. For telephone network design including modern synthesis filters, delay equalizers, discriminator networks, loss and phase equalizers, transistor switching circuitry etc.
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3. General communications equipment design and development.

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1. Experience in carrier engineering; knowledge of dial and manual telephone systems.
2. For systems engineering work required by telephone central office equipment.

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PhD or outstanding MS in Math, Physics or EE. Specialist in information theory applied to communications and data systems.

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EE degree or equivalent; technical writing experience. To work on military publications. Must be capable of working with schematics, electronic equipment and specifications to derive theory and maintenance information.

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2. Undersea Warfare (airborne and submarine sonar systems).
3. Digital Computer Systems (airborne navigation and missile guidance).
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2. Advanced automatic test equipment.
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1. PhD or MS in EE or Physics. To supervise and act as consultant and liaison specialist in systems design work—both theoretical and equipment—in broad communications projects.

2. To supervise integration of antennas (emphasis on broadband ECM receiver types) into an ECM reconnaissance system.

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Experience in systems theoretical design and/or equipment design. Requires knowledge of entire electromagnetic spectrum; working knowledge of propagation methods.

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(Continued from page 156A)

in the millimeter waveguide ranges has been developed by the Narda Microwave Corp., 118-160 Herricks Rd., Mineola, N. Y.



Specific equipment in K, V, Q, M, and E Bands which is now available includes Variable Waveguide Attenuators, Tunable Waveguide Detectors, High Directivity Directional Couplers, Impedance Meters, VSWR Amplifiers, Terminations, E-H Tuners, Frequency Meters, and Waveguide Clamps and Stands.

Particular care is taken in each step of the fabrication to assure the additional precision required for the higher frequency ranges encountered. For example, silver or tellurium copper is used as waveguide material to maintain transmission losses at a minimum. Similar precautions are taken with all other millimeter components to insure their complete reliability.

Dual Feed Horn

A dual polarized feed horn for large size waveguide having two waveguide inputs has just been developed and put into use by D. S. Kennedy & Co., Cohasset, Mass. The unique feature of this primary feed is the waveguide input, since the usual dual polarized horn requires a coax input.



The new feature has the advantage of providing the same center of radiation for both signals. Maximum power transmission is obtained in both polarizations. The horn handles 10 kw with more than 30 db decoupling between the signals.

The horn has been produced in the frequencies of 1700-2400 mc, 755-985 mc and 400-450 mc, but the design is available in other frequencies. For further information contact the firm.

Crystal Controlled Signal Generator

The Model 46-A High Level Crystal Controlled Signal Generator designed by Ferris Instrument Co., Boonton, N. J., de-

(Continued on page 160A)

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Communication & Navigation
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Chemistry Laboratory
Antenna & Radiation Systems
Applied Physics Laboratory
Analysis & Computation Laboratory

Positions are also available in our Production Division and our Quality Control Department.

For details about opportunities at Melpar,
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Positions exist in Engineering Department which is engaged in advanced design and development of military weapons and reconnaissance systems, communications, controls, guidance, navigation, and special purpose digital computers. Work is mainly military, with some special commercial instrumentation and control.

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NEWS New Products



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(Continued from page 158A)

livers at least 2 watts of rf power into a 50 ohm load at precise frequencies of 5, 10, 50 and 100 mc. It may be used as a sub-



stitute for WWV in those areas where it is difficult to receive signals over a 24 hour period. All frequencies stem from a 5 mc temperature controlled Ultra High Stability Crystal with a rated frequency stability of 0.00001 per cent over short periods, and 0.0001 per cent long time stability. For additional details, write to the firm.

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Copies of Bulletin 385A are available from the firm.

Magnetic Amplifier Bulletin

Acromag, Inc., 22519 Telegraph Rd., Detroit 41, Mich., has a new 2 color, 4 page bulletin describing their standard series 400 cps precision magnetic amplifiers. These amplifiers are used for such applications as missile guidance, automatic pilots, industrial controls, monitoring systems, helicopter rotor speed controls, nuclear measurements and electro-hydraulic servo valves. Included in the new bulletin are two pages of drawings showing basic circuits and typical applications. Bulletins available on request.

High Reliability Electrolytics

Type QE, Computer-Grade electrolytic capacitors are precisely engineered for high reliability and long operating life by Aerovox Corp., New Bedford, Mass. They are designed specifically for such critical applications as computer equipment, power supply filters, telephone networks,

(Continued on page 162A)

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SENIOR ENGINEERS
ENGINEERS
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We need at once for lifetime careers—additional trained personnel, at all levels, experienced in circuitry and equipment design or applicable exp. to work on UHF & VHF systems, wide band knowledge desirable; for challenging assignments on electronic counter-measure systems for military application and electronic instruments for civilian use.

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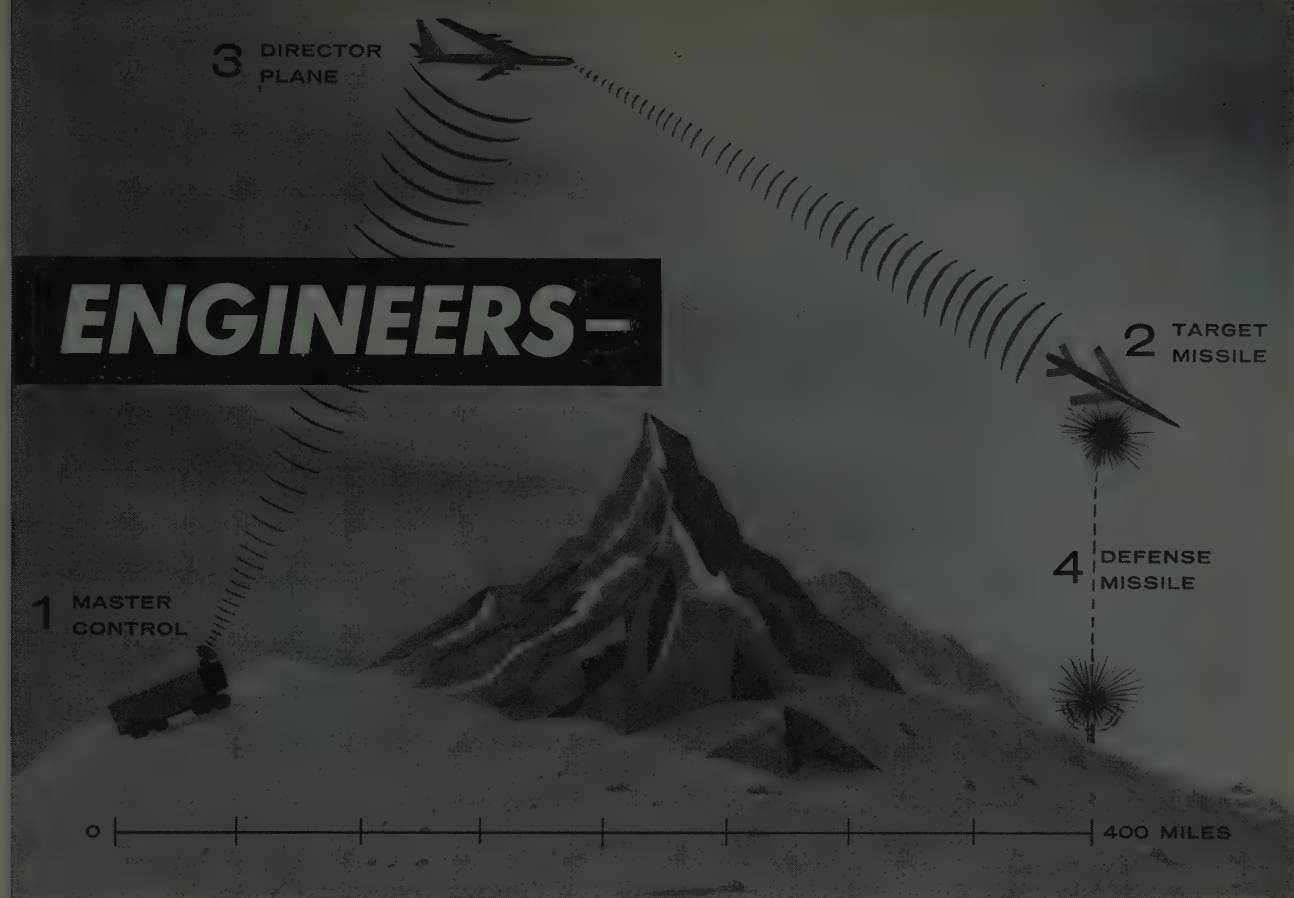
N. L. Jochem, Director of Engineering
Box P-4

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on challenging assignments
like this...**

In action Sperry system, housed in air-transportable trailer (1), can command, track and telemeter drone flight data of supersonic target (2) either directly or through air director (3) when either long range or low altitude is involved. Object is to test readiness of anti-missile defense and accuracy of ground-to-air defense missile (4)

DRY RUN FOR USAF ANTI-MISSILE DEFENSE

New Sperry radar guidance system controls drones at 400-mile range

A microwave command guidance system designed to help test U.S. defenses against potential enemy weapons has been successfully demonstrated to the Air Force. Developed by Sperry under contract with the Air Research and Development Command, the system is scheduled for initial use with Q-4A supersonic drones.

Just one of many projects of vital importance that Sperry engineers work on. Advanced electronic and gyroscopic systems connected with Polaris Missile, integrated countermeasures systems, Terrier, Tartar, Talos radar guidance systems, Tactical early warning radar systems, Ship gyro stabilizers... the list of Sperry projects is almost endless.

No wonder Sperry is thought of as an "engineer's firm." It offers the kind of diversified, important assignments that attract and hold career engineers. Proof of this is found in the fact that over 2,600 Sperry Employees are 15-year men.

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Boonton, N.J. DE 4-1800—Ext. 238



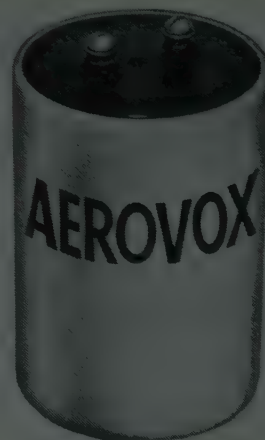
NEWS New Products



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(Continued from page 160A)

Industrial electronic equipment and precision laboratory and commercial test equipment.



QE capacitors have a useful life expectancy of greater than 10 years when operated within ratings. Operating life will further improve when the ambient temperature is below 65°C. Units are rated for operation at temperatures from -20°C to +85°C. Manufactured in drawn aluminum cases in four diameters and one standard 4½ inch height to facilitate busbar connections for purposes of gauging in banks.

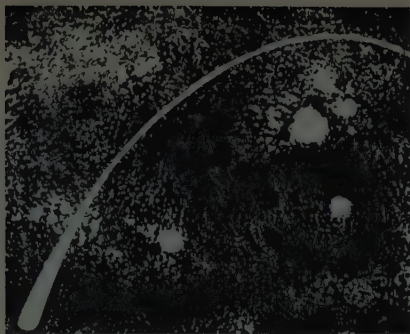
These remarkable new capacitors are the result of more than 30 years experience in the manufacture of hundreds of millions of electrolytic capacitors. For complete technical information write to the Applications Engineering Department.

TWT Gives 100 Milliwatts Output At 55,000 MC

A traveling wave tube which provides CW powers of 100 milliwatts or more at 55,000 mc with a bandwidth of 10,000 mc is in an early stage of development at Bell Telephone Laboratories. The tube was described at the annual convention of the IRE Professional Group on Electron Devices in a paper prepared by W. E. Danielson, H. L. McDowell and E. D. Reed of Bell Telephone Laboratories, 463 West Street, New York 14, N. Y.

Interest in frequencies in this range has been sparked by the possibility of long distance transmission at millimeter wavelengths using a circular electric mode in round waveguide pipe buried in the ground. The tube described is intended for use as a power amplifier in such a communication system. It has produced ten times more CW power output than has previously been reported for any other amplifier at this frequency.

(Continued on page 164A)



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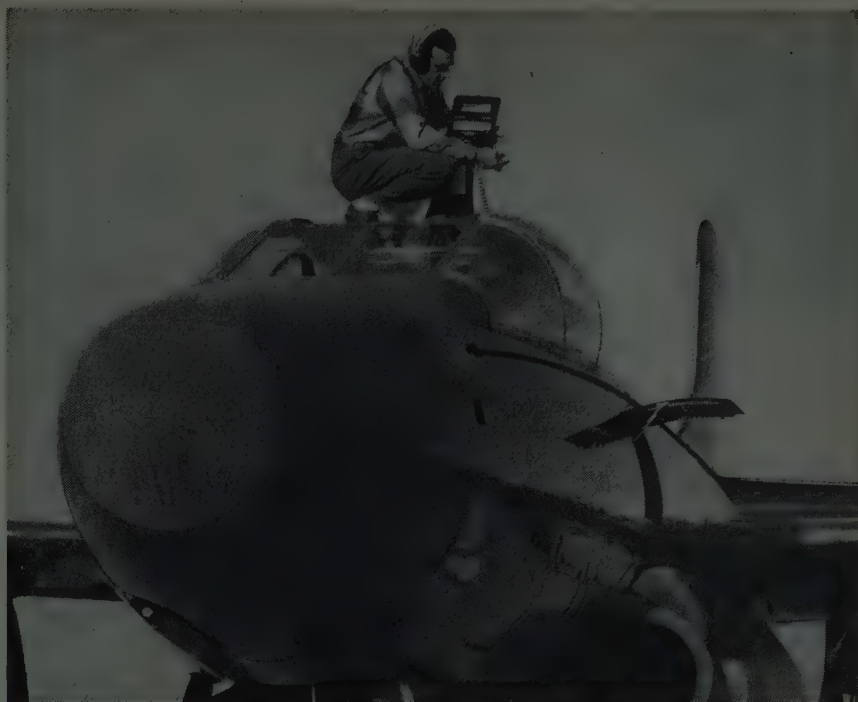
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DESIGN**

ANTENNA DESIGN

ELECTRONIC PACKAGING

**SYSTEMS ANALYSIS &
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TECHNICAL WRITING

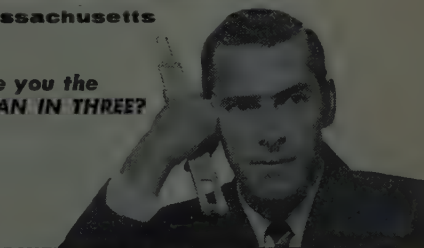
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ADVANCED CIRCUIT DESIGN

For complete details on engineering positions in any of Maynard's project groups, please write John J. Oliver, P.O. Box 87P, Raytheon Maynard Laboratory, Maynard, Mass.

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Excellence in Electronics

This is one of a series of professionally informative messages on RCA Moorestown and the Ballistic Missile Early Warning System.

BMEWS AND THE DEVELOPMENT ENGINEER

The Ballistic Missile Early Warning System will be the keystone of defense against enemy-launched ICBM's. The development and design engineer assigned to BMEWS will determine to a great extent the future security of the Western Hemisphere, for the successful functioning of this unique radar system will depend upon his ability to translate technological concepts into effective hardware. On BMEWS the development and design engineer must project advanced theories of analog and digital computing and data handling systems, cathode-ray or electroluminescent display systems, or any of the many facets of radar into circuits and components. He must have the analytical capability and imagination to achieve the advanced performance necessary for BMEWS.

BMEWS development is currently in progress at RCA Moorestown, the weapon system manager, and also within the facilities of several other major corporations whose efforts are coordinated by RCA. Entering the BMEWS program at an early date will afford engineers the opportunity to contribute to the basic system development and, through continuing participation, to witness its evaluation into a final operating equipment.

For further information concerning career engineering opportunities on BMEWS and other defense programs at RCA Moorestown, please direct your inquiry to Mr. W. J. Henry, Box V-17M.



RADIO CORPORATION OF AMERICA

MISSILE AND SURFACE RADAR DEPARTMENT

MOORESTOWN, N. J.

These manufacturers have invited PROCEEDINGS readers to write for literature and further technical information. Please mention your IRE affiliation.

(Continued from page 162A)



H. L. McDowell (left) and L. J. Speck (holding tube) of Bell discussing the tube. Background equipment is for evacuating and testing.

In this tube a 7000 volt, 3 milliamperes electron beam is projected through a 4 inch long helix having a bore of only 15 mils. This helix is made from copper-plated molybdenum wire wound at 110 turns per inch. With a magnetic focusing field of about 1500 gauss, the beam current intercepted by the helix is held to 5 per cent or less. A converging electron gun is used so that cathode current density is held to about 1 ampere per square centimeter—a value which should make a cathode lifetime of thousands of hours possible.

Although similar in principle to helix type traveling wave tubes used at lower frequencies, the millimeter wave tube required a completely new design approach because of the small sizes involved. The helix is glazed to a single support rod of low-loss ceramic instead of the more conventional three rods. This rod is spring-loaded against a heat sink which has a direct heat conduction path to the outside of the vacuum envelope. The required degree of precision is obtained by a combination of optical alignment techniques and specially selected machining operations. In this manner, tolerances of the order of one-ten-thousandth of an inch can be maintained with piece part tolerances which are, for the most part, an order of magnitude less severe.

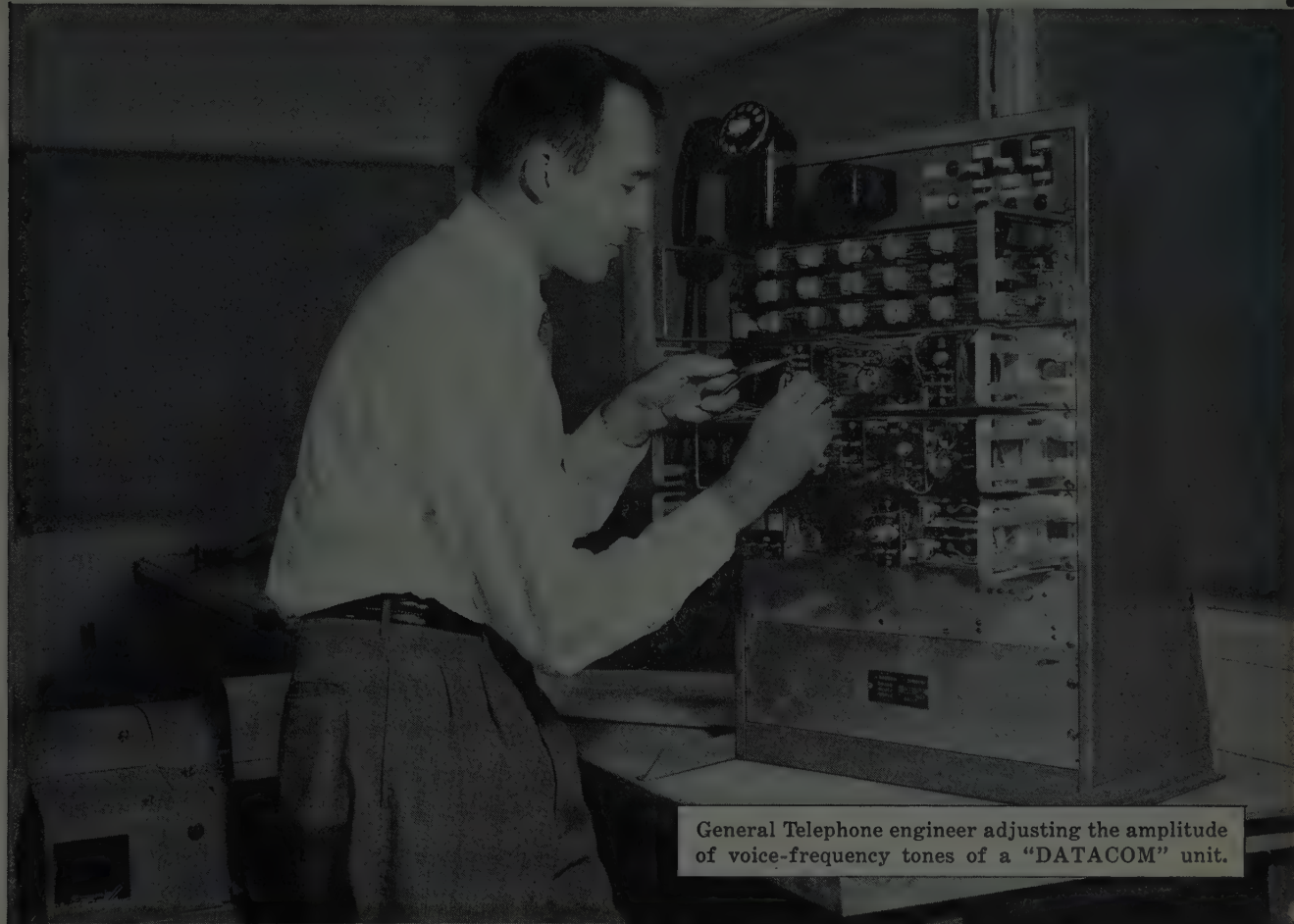
Experimental tubes have been tested at 55 kmc and have given CW output powers ranging from 125 to 200 milliwatts. Gain at maximum output is 19 db and at low level is 25 db. These results show that the basis has been laid for a practical broadband traveling-wave amplifier with CW power outputs of 200 milliwatts or more at 55 kmc.

Transistorized Frequency Shift Keyer and Converter

By transistorized circuitry and concomitant compact design, Northern Radio Co., Inc., 147-49 W. 22nd St., New York 11, N. Y. has been able to achieve 18 channels of FS Tone Telegraph keying equipment in panel space only 19 wide x 5 1/2 high x 18 inches deep, and 18 channels of

(Continued on page 166A)

The GENERAL idea on Engineering Careers



General Telephone engineer adjusting the amplitude of voice-frequency tones of a "DATACOM" unit.

We've "taught" computers to talk on the phone

Giving voice to electronic data processing equipment so it can "talk over the phone" is one of the many fascinating projects completed or in development by engineers at General Telephone Laboratories.

In essence, the Digital Data Communication Set permits the two-way transmission of digital information over telephone lines in much the same manner as ordinary conversation.

How does it work? The "DATACOM" accepts sequential binary data from the computer and modulates the d-c pulses to FM signals acceptable to telephone channel band widths. These signals are transmitted to the line, detected at the receiving end and reconverted to d. c. serialized binary data. The system is applicable to either digital or teletypewriter equipment.

This is but one of the many challenging projects in communications and automatic control open to enterprising physicists and engineers at General Telephone Laboratories.

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If you have a Doctorate in Physics, Electrical Engineering or Mechanical Engineering and seek your future in the research and design of electronic or electromechanical systems, we have a particularly attractive opening for you. For more specific details write, in confidence, to Mr. Robert Wopat, President, General Telephone Laboratories, Northlake, Illinois.

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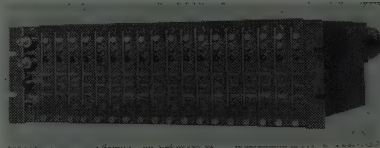
NEWS New Products

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(Continued from page 164A)

FS Tone Telegraph converter equipment in panel space only 19 wide \times 10½ high \times 18 inches deep.

Keyer



Keying inputs, levels and impedances
(1) Contact keying (internal battery to "dry" contacts) 1 ma min; (2) dc current pulses, positive or negative, neutral or polar, high range, 220 ohms, 30 ma min low range, 2200 ohms, 0.5 ma min; (3) dc voltage pulses, positive or negative, neutral or polar, high range, 100,000 ohms, 10 volts min, low range, 2200 ohms, 1 volt minimum.

Frequency stability: Standard Networks ± 2 cps total for all causes including ± 10 per cent line voltage change and $\pm 25^\circ\text{C}$ from 25°C temperature change.

Harmonic content: All harmonics of the tone are more than 50 db below output level.

(Continued on page 168A)

P H O N I X

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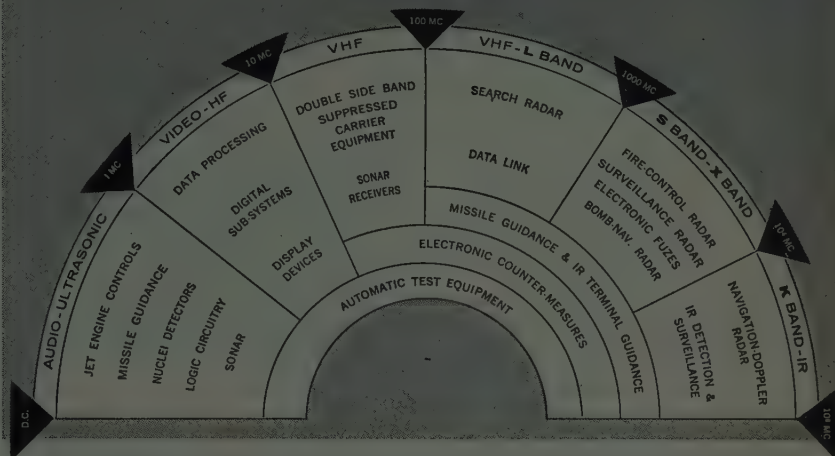
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NEWS New Products



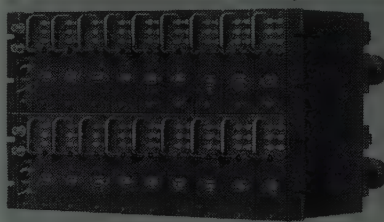
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(Continued from page 166A)

Output Frequencies: All standard VF carrier channels from 425 to 3315 cps. Bandwidth dependent on keying speed requirements. Other frequencies and bandwidths available on special order.

Output level and impedance: ± 5 dbm maximum, into 600 ohms, unbalanced. May be paralleled with any number of other keyers operating on different frequencies in the same audio systems.

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Input Level and Impedance: -48 dbm to $+8$ dbm into 600 ohms, unbalanced. May be paralleled with any number of other converters operating on different frequencies in the same audio system.

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Output: Neutral DC voltage pulses of 10 volts maximum across a 2000 ohm external load. Polar pulses ± 10 volts across a 2000 ohm external load. Output drives appropriate voltage-to-current converters, such as Northern Radio Type 213 Transistor Relay, which provides proper teleprinter operating currents. Printers which are already equipped with internal repeating relays may be driven directly from the normal voltage output terminals of the Type 212 Converter when so desired.

Electronically Variable Attenuator



This broadband coaxial attenuator, called V PAD, by its manufacturer, Microwave Control Corp., 250 W. 57th St., New York 19, N. Y., is electronically variable from 10 to 25 db. The variation is continuous, being a function of the solenoid current, with the maximum attenuation requiring 30 ma at S band and 70 ma at X band. Other models are available with attenuation as low as 3 db over the 2-10 kmc range. Featuring low VSWR, light in

(Continued on page 170A)

ELECTRONIC ENGINEER

(Senior)

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Of Illinois Institute of Technology

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(Continued from page 168A)

weight, small in size, having no moving parts, V PAD offers increased versatility for buffer and pad applications in signal generator, search receiver and power measuring circuits. Being electronic, this coaxial device also serves as an amplitude modulator for microwave rf.

Double-Diffused Silicon Rectifiers

Double diffusion processed silicon rectifiers in the Jetec series 1N536 through 1N540 and in the Jetec series 1N2080 through 1N2086 have been released by the Semiconductor Manufacturing Div., Columbus Electronics Corp., 1010 Saw Mill Rd., Yonkers, N. Y.



Available in the familiar, hermetically sealed, axial lead top hat design, the units achieve high rectification efficiency through a desired combination of low forward drop and low leakage currents. In addition, these semiconductor devices withstand high overload currents. Other features include 500 to 750 ma rectified current and up to 600 peak inverse volts without heat sink.

Specifications and literature are available by writing Sales Manager, Columbus Electronics Corp.

New Douglas Division

Douglas Microwave Co., Inc., of Mt. Vernon, N. Y., announces the formation of its newest division to be known as Spectra Electronics Corp., with offices and laboratories at 250 E. Third St., Mt. Vernon, N. Y. The new corporation will specialize in creative research, development and precision manufacture in the fields of space electronics, guidance, data processing and acquisition systems, special test equipment, infrared instrumentation and systems, radar instrumentation, telemetry, countermeasures, security systems and communications—serving industry and government.

Spectra executive personnel includes R. Harry Douglas, Senior Systems Analyst; Herbert M. Hendlin, Engineering Manager; Edward J. Warner, Manager, Ap.

(Continued on page 172A)

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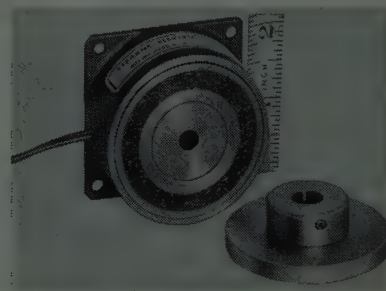
(Continued from page 170A)

lications Engineering and Senior Systems Analyst; and D. J. Lovell, Director of Engineering.

A descriptive brochure may be obtained by contacting: Spectra Electronics, Dept. P-1, 250 E. Third St., Mt. Vernon, N. Y.

Coupling Type Clutch

Stearns Electric Corp. 120 N. Broadway, Milwaukee 2, Wis., is pleased to announce the availability of a flange mounted, stationary field, coupling type clutch for applications having a minimum of space available.



This unit is furnished with a mounting flange $2\frac{1}{2}$ square and $1\frac{9}{16}$ inches long, including armature and driven hub, and 1 inch long without armature and driven hub. It can be offered with a coil suitable for operation on any dc source with voltages up to 90 volts dc. It has a static torque rating of 30 inch pounds.

For further information contact Robert Kirk at the firm.

Plug-In VTVM Circuitry

Plug-in electronic voltmeter circuitry, intended for applications where metering and range switching must be remote, has been developed by Metronix, Inc., Chesterland, Ohio.



(Continued on page 174A)

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(Continued from page 172A)

Model SPD-21 is a dc package that may be used with other components to measure from 1 to 1000 volts. It contains complete VTVM circuitry but does not include the meter, calibration control, zero adjust, or the input voltage divider that selects the voltage range desired.

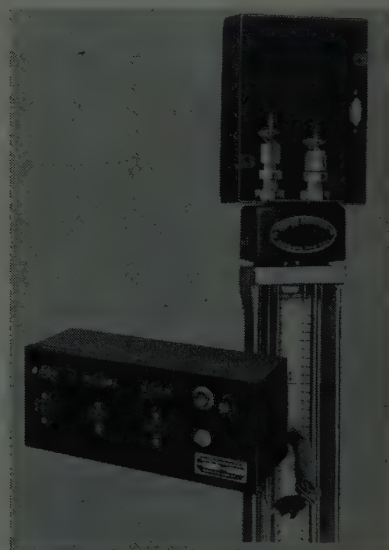
With this unit, meters being utilized for other purposes may also be used for electronic voltage measurement.

Model SPD-21 occupies $4\frac{1}{2}$ square inches in cross section. Dimensions are 2 by $2\frac{1}{4}$ by $5\frac{1}{4}$ inches.

With an input resistance of 10 megohms, Model SPD-21 imposes almost no load on the circuit being measured. Its accuracy is ± 3 per cent. Meters used with the circuit should have a minimum sensitivity of $250 \mu\text{a}$, maximum of $50 \mu\text{a}$. Input power required is 115 volts, 50 to 400 cps, single phase.

Pressure Switch

A new precision pressure switch capable of accurate and sensitive response has been developed by the Meriam Instrument Co., 10775 Madison Ave., Cleveland 2, Ohio. Consisting of a contactor manometer and a relay-power-supply package (tradenamed Manotac), the unit may be used for alarm signalling and/or control in applications involving pressure, vacuum, differential pressure, flow and liquid level.



The use of a special indicating fluid (Sp. Gr. equals 1) gives a make-or-break control sensitivity of 0.005 inch of water; the instrument can sense pressure increments as small as 0.003 ounce per square inch with complete dependability.

Switching functions are handled by the Manotax Relay-Power Unit, which operates at 110 v ac. It features modular construction that makes use of interchangeable plug-in circuit cards. Each carries all components governing one contact point

(Continued on page 176A)



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The system concept demonstrated in the "Sergeant" has permitted excellent mobility and speed of operation to be attained. The requirements of the Army have been stressed, resulting in outstand-

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NEWS New Products



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(Continued from page 174A)

on the manometer and may be removed or inserted without affecting operation of other points. Individual load relays are fully enclosed and have dpdt switching action. Manotac units are made in two types: plug-in for quick, temporary connections, and tamper-proof for permanent monitoring or control applications. Both are available in five models designed for from one to five contact points. Contact capacity is 5 amperes per point at 115 volts, ac.

For full information, request Bulletin A-11 from the firm.

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Advertising Index

IRE News and Radio Notes	14A
IRE People	30A
Industrial Engineering Notes	64A
Meetings with Exhibits	8A
Membership	70A
News—New Products	22A
Positions Open	134A
Positions Wanted by Armed Forces Veterans	130A
Professional Group Meetings	60A
Section Meetings	78A
Table of Contents	1A-2A

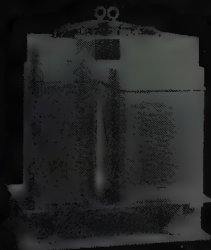
DISPLAY ADVERTISERS

A C Electronics Div., General Motors Corp.	143A
Abbot, Edward A.	176A
Abbott's Employment Specialists	151A
Accredited Personnel Service	174A
Ad. Auriema, Inc.	155A
Aeronutronic Systems, Inc.	162A
Airborne Instruments Lab.	4A
Aircraft Radio Corp.	87A, 162A
All Products Company	40A
Allen-Bradley Company	52A-53A
American Electrical Heater Co.	114A
American Television & Radio Co.	42A
Amperex Electronic Corp.	104A
Amphenol Electronics Corp.	26A
Andrew Corporation	81A
Ansley, Arthur C.	176A
Armour Research Foundation, Illinois Inst. of Technology	132A, 170A
Armstrong Whitworth Aircraft, Sir W. G.	120A
Arnoux Corporation	112A
Autonetics Div., North American Aviation, Inc.	169A
Avco Mfg. Co. Avco Research & Advanced Development Div.	173A

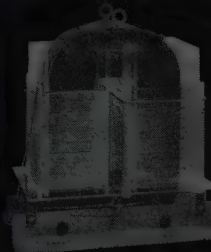
Baldwin Piano Co., Industrial Products Div.	10A
Ballantine Laboratories, Inc.	56A
Baracket, Albert J.	176A
Beede Electrical Instrument Co., Inc.	68A
Bell Telephone Laboratories	6A
Belleville-Hexem Corporation	58A
Bendix Aviation Corp., Bendix-Pacific Div.	156A
Bendix Aviation Corp., Guided Missile Section	130A
Bendix Aviation Corp., Kansas City Div.	171A
Bendix Aviation Corp., Research Labs. Div.	142A
Bendix Aviation Corp., York Div.	163A
Bickel, Richard L.	176A
Bliley Electric Co.	106A
Boeing Airplane Company	139A
Boesch Mfg. Co., Inc.	108A
Bomac Laboratories, Inc.	17A
Boonton Radio Corp.	66A
Bourns Laboratories, Inc.	93A
Buckbee Mears Company	34A
Burlingame Associates	46A
Burnell & Company, Inc.	19A
Bussmann Mfg. Div., McGraw Edison Co.	57A

CBS—Hytron Div.	47A
Caledonia Electronics & Transformer Corp.	108A

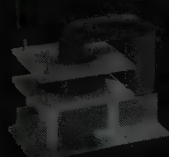
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Secondary Peak Current	220 Amperes
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Rise Time	0.3 μ sec.
Droop	2.5%
Repetition Rate	180 PPS
Load	Klystron, 1250 Ω
Size, Weight	10" x 18" x 22½" high; approx. 200 lbs.

817- PULSE TRANSFORMER	
Secondary Peak Voltage	250 KV maximum
Secondary Peak Current	234 Amperes max.
Turns Ratio	1:17
Pulse Width	3 - 8 μ sec.
Rise Time	0.5 μ sec. min., 1.0 μ sec. max.
Droop	1.5 KV per μ sec. of pulse length max.
Repetition Rate	360 PPS max.
Load	Klystron, 1070 Ω
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922 FILAMENT TRANSFORMER	
Primary Voltage	208 V, 60 cycles
Secondary Voltage	18 V at 10 Amps.
Insulation Voltage	260 KV Pulse
Capacitance	40 μ mf in oil, approx.
Size, Weight	9" x 12.5" x 10" high; approx. 40 lbs.

814 PULSE COUPLING TRANSFORMER	
Secondary Insulation	220 KV DC
Primary/Secondary Turns Ratio	1:2
Primary Voltage	4 KV; Secondary Voltage 8 KV
Secondary to Primary & Core Capacitance	50 μ mf approx.
Pulse Length & Rate	2-5 μ sec. 60 PPS max.
Pulse Droop, Overshoot, Backswing	15%
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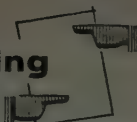
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Advertising Index



Capitol Radio Engineering Institute	50A
Carad Corporation	177A
Ceramaseal, Inc.	118A
Clevite Transistor Products	154A
Cohn Corporation, Sigmund	106A
Collins Radio Company	35A, 150A
Communication Products Co., Inc.	108A
Computer-Measurements Corp.	126A
Consolidated Avionics	71A
Consolidated Mining & Smelting Co.	80A
Cornell Aeronautical Lab., Inc.	146A
Cornell-Dubilier Electric Corp.	Cover 3
Corning Glass Works	49A
Curtiss-Wright Corporation	65A, 156A, 170A

D & R, Ltd.	126A
Dale Products, Inc.	60A-61A
Delco Radio Div., General Motors Corp.	97A
DeMornay-Bonardi	74A
du Pont de Nemours & Co., Inc., E. I.	99A

EIC	120A
E S C Corporation	63A
Eastern Industries, Inc.	55A
Ehrenfried, A. D.	176A
Eitel-McCullough, Inc.	41A, 107A
Ekstrom, Joel L.	176A
Electronic Associates, Inc.	68A
Electronic Research Associates, Inc.	8A
Elgin National Watch Company	25A
Empire Devices Products Corp.	72A

F-R Machine Works, Inc.	facing 32A-33A
Food Machinery & Chemical Corp.	151A
Freed Transformer Co., Inc.	58A
Frequency Standards	117A

Gates Radio Company	160A
General Electric Co., Electronics Laboratory ..	136A
General Electric Co., Light Military Electronics Dept.	167A
General Electric Co., Power Tube Dept.	94A-95A
General Electric Co., Technical Products Dept.	24A
General Mills, Inc., Mechanical Div.	123A, 140A
General Radio Company	Cover 4
General Telephone Labs.	165A
Gilfillan Brothers, Inc.	166A
Goodyear Aircraft Corp.	166A
Guilford Personnel Service	155A

Hallcrafters Company	50A
Hallmark, Clyde E.	176A
Heath Company	90A
Hewlett-Packard Company	21A, 85A
Hickok Electrical Instrument Co.	88A
Huggins Laboratories	98A
Hughes Aircraft Company	144A-145A
Hughes Products	89A
Hycon Eastern, Inc.	96A

ITT Laboratories, Div. Intl. Tel. & Tel. Corp.	167A
Institute of Radio Engineers	5A, 86A, 102A
Instruments for Industry, Inc.	160A
International Business Machines Corp.	137A
International Rectifier Corp.	59A
International Telephone & Telegraph Corp., In- dustrial Products Div.	111A

Advertising Index

International Telephone & Telegraph Corp., ITT
Components Div.31A
International Telephone & Telegraph Corp., ITT
Laboratories Div.167A

Jet Propulsion Lab., Calif. Inst. of Technology 175A
Johns Hopkins University, Applied Physics Lab. 82A
Johns Hopkins University, Operations Research
Office158A
Jones Div., Howard B., Cinch Mfg. Corp.112A

Kahn, Leonard R.176A
Kay Electric Company9A
Kearfott Company, Inc.36A, 154A
Kennedy & Company, D. S.43A
Kepco Laboratories, Inc.80A
Knights Company, James179A
Knopow, Howard S.176A
Kollsman Instrument Corp.136A
Krohn-Hite Corporation70A

Lambda Electronics Corp.29A
Lapp Insulator Co., Inc.38A
Link Aviation, Inc.147A
Litton Industries, Electronic Equipments Div. 134A
Litton Industries, Maryland Div.155A
Lockheed Aircraft Corporation131A

Magnavox Company135A
Magnetics, Inc.27A
Marconi Instruments178A
Martin Company42A
Mass. Inst. of Technology, Lincoln Lab.166A
Mayberry, Len176A
McCoy Electronics Co.48A
Measurements, A McGraw Edison Div.180A
Melpar, Inc.159A
Menlo Park Engineering120A
Microwave Associates, Inc.92A
Millen Mfg. Co., Inc., James64A
Moseley Company, F. L.122A
Moskowitz, S., D.D. Grieg176A
Motorola, Inc., Semiconductor Products Div.51A
Motorola, Inc., Western Military Electronics
Center168A
Mucon Corporation34A

National Aeronautics & Space Administration 103A
National Cash Register Co.152A
Nixon, V. J., S. K. Wolf, M. Westheimer176A
Norden Labs., Norden Div., United Aircraft
Corp.138A
North American Aviation, Inc.140A, 169A
Northern Radio Company, Inc.124A-125A

Ohio Semiconductors, Inc.39A
Oldsmobile Div., General Motors Corp.109A
Ordnance Research Lab., Penn. State Univ.172A
Oster Mfg. Co., John32A
Ostlund, Evert M.176A

Pacific Semiconductors, Inc.101A, 150A
Pan American World Airways, Inc.142A
Panoramic Radio Products, Inc.127A
Parke, Nathan Grier176A
Perkin Engineering Corp.11A

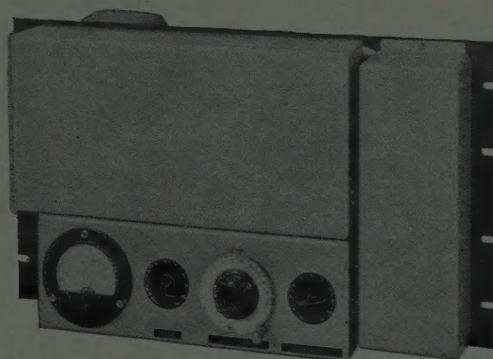


CRYSTAL CONTROLLED OSCILLATORS

with performance certified for each
unit on printed digital tape record

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Crystallography, electronic circuitry, thermal and mechanical design integrated and optimized to provide maximum stability and reliability, with minimum size and weight.



PRECISION FREQUENCY STANDARDS

Time-Proven JKFS-1000

Stability: 1×10^{-9} /Day

Output: 5 V into 5000 ohms at 1 mc; 500 kc and 100 kc. Pulse output for measurements up to 20 mc

The new JKFS-1100-T

Stability: 5×10^{-10} /Day

Fully Transistorized: Built-in battery standby power source for 20 hours of operation

Output: 1 V into 50 ohm-load at frequencies of 1 mc and 100 kc.

Dimensions: $8\frac{3}{4}'' \times 19''$ panel for rack mounting

PLUG-IN FREQUENCY STANDARDS—1MC

JKTO-P1A

Stability: 1×10^{-7} /Day.

Output: 1 V into 50,000 ohms.

Power: Operates from 24 to 28V D.C.

Oven: Long life; booster and control thermostats hermetically sealed.

Dimensions: $1.8'' \times 2'' \times 3''$ H; Wt. 9 oz.

Environmental: Hermetically sealed; meets aircraft equipment specifications with frequency stability of 4×10^{-7} .

NEW JKTO-PIP

Stability: 1×10^{-8} /Day

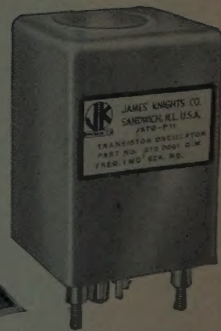
Oven: Transistorized proportional control oven with fast warm-up and precise temperature control.

Output: 1 V into 5,000 ohm-load.

Power: Operates from 24 to 28V D.C.

Dimensions: Max. $1\frac{3}{4}'' \times 2\frac{3}{8}'' \times 3\frac{1}{4}''$ H; Wt. 10 oz.

Environmental: Hermetically sealed; meets aircraft equipment specifications with frequency of 4×10^{-8} .



A WIDE RANGE OF JKTO PLUG-IN REFERENCE OSCILLATORS

Stability: 1×10^{-6} /Day

Frequency Range: 50 cycles to 50 mc

Oven: Features long-life, new "Snap-Action" thermostat

Write for literature, giving model number, and state your specific requirements.

THE JAMES KNIGHTS COMPANY
Sandwich, Illinois

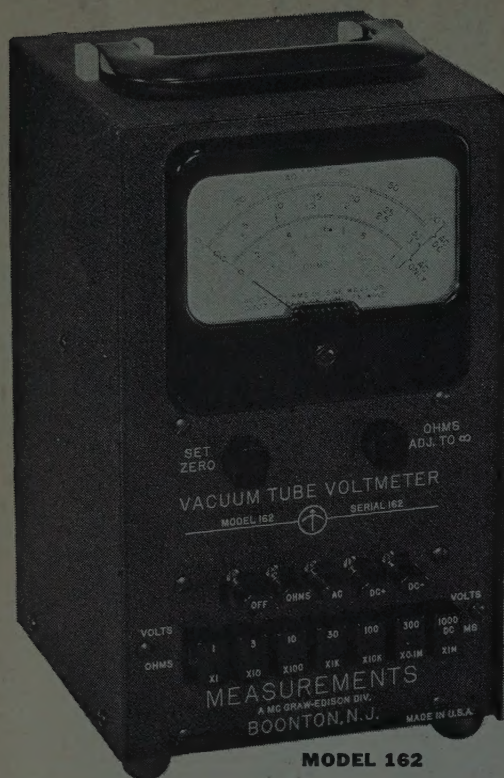
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NEW

VACUUM

TUBE

VOLTMETER



MODEL 162

Provides RANDOM ACCESS to all functions and ranges through the use of push-button switches.

- For voltage and current measurements in laboratories, service shops and on production lines.
- For accurate rf and ac voltage measurements from 0.1 to 300 volts on electronic equipment from the low audio range through the VHF range.
- For dc voltage measurements from 0.01 to 1000 volts without disturbing circuit performance.
- For direct current measurements as low as 0.001 microamperes.

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Laboratory Standards



MEASUREMENTS
A McGraw-Edison Division
BOONTON, NEW JERSEY

STANDARD BOLOMETER BRIDGE

The Most Accurate Means of Calibrating
High Frequency Voltages



MODEL 202-C

Wide frequency range—2 Mc to 1000 Mc... True RMS response... High accuracy, excellent stability and sensitivity... Bolometer element in temperature-controlled oven... 50 ohms impedance with VSWR less than 1.2.

WRITE FOR BULLETIN

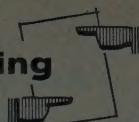
Laboratory Standards



MEASUREMENTS
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BOONTON, NEW JERSEY



**Advertising
Index**



Permanent Employment Agency171A
Philco Corp., Lansdale Tube Co. Div.126A
Polarad Electronics Corp.facing 68A-69A

Radio Corp. of America, Semiconductor and
Materials Div.100A
Radio Corp. of America, Specialized Employment
Div.151A, 164A
Raytheon Mfg. Co., Magnetic Components
Dept.78A
Raytheon Mfg. Co., Microwave & Power Tube
Div.23A
Raytheon Mfg. Co., Personnel Recruitment
.....133A, 163A
Raytheon Mfg. Co., Semiconductor Div.37A
Reeves-Hoffman Div., Dynamics Corp. of Amer-
ica40A
Republic Aviation Corp.168A
Rider, Publisher, Inc., John F.30A
Rixon Electronics, Inc.114A
Rosenberg, Paul176A

Sanborn Company73A
Sangamo Electric Company129A
Schachter, Jacob176A
Scientific-Atlanta, Inc.84A
Shockley Transistor Corp.159A
Singer Mfg. Co.115A
Sola Electric Company20A
Sorensen & Company, Inc.52A
Space Technology Labs., Div. Ramo-Wooldridge
Corp.12A, 153A
Specific Products118A
Sperry Electronic Tube Div., Sperry Rand Corp. 140A
Sperry Gyroscope Co., Div. Sperry Rand Corp. 161A
Spittal, William R.176A
Sprague Electric Co.3A, 7A, 69A
Stoddart Aircraft Radio Co., Inc.76A
Stromberg-Carlson Company53A, 116A, 157A
Superior Cable Corp.54A
Switchcraft, Inc.122A
Sylvania Electric Products Inc. .33A, 75A, 148A-149A

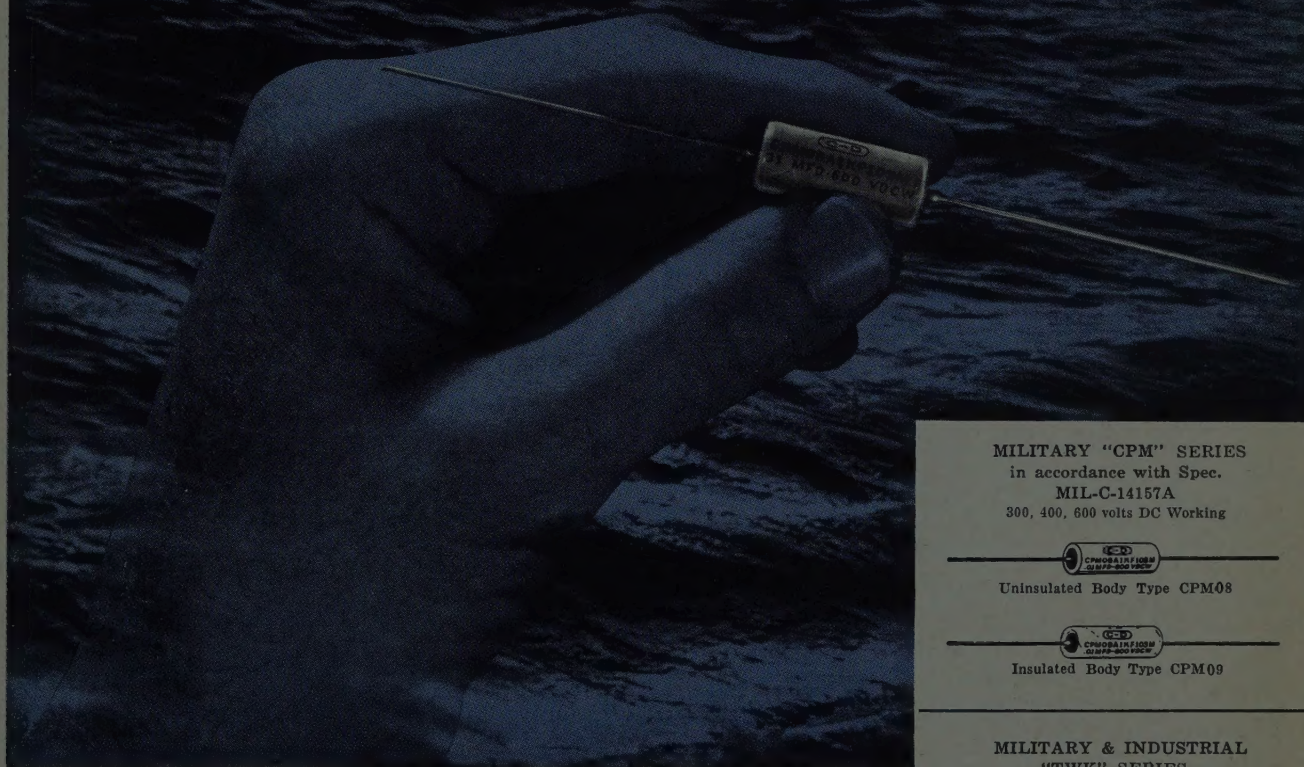
Tarzian, Inc., Sarkes110A
Tektronix, Inc.28A
Telecomputing Corp.91A
Temco Aircraft Corporation121A
Texas Instruments Incorporated .44A-45A, 77A, 141A
Thompson-Ramo-Wooldridge, Inc.12A-13A
Thompson-Ramo-Wooldridge Products Co.
.....119A, 132A
Tung-Sol Electric, Inc. .67A, 79A, 105A, 154A, 171A

United Transformer Co.Cover 2
University of Arizona136A

Varian Associates62A

Wallace, Don C.176A
Ward Leonard Electric Company83A
Welwyn International, Inc.128A
Western Devices, Inc.116A
Westinghouse Electric Corp.168A
Weston Instruments, Div. Daystrom, Inc.113A
Wheeler, Harold A.176A
White Industrial Div., S. S.84A
Winner, Lewis176A

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Cornell-Dubilier Certified High-Reliability Capacitors meet performance expectations for new environments and new complex military and industrial electronic equipment. These capacitors meet or surpass the exacting requirements of MIL-C-14157A and MIL-C-26244 (USAF). Each production lot is furnished with certified test data covering the stringent test program detailed in the specification.

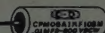
When designing electronic equipment where *failure can't be tolerated* specify Cornell-Dubilier High-Reliability Capacitors. Write on your company letterhead for High-Reliability Bulletins 188A-1 and 188A-2 to Dept. IR-12, Cornell-Dubilier Electric Corporation, South Plainfield, New Jersey.

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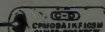
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MIL-C-14157A

300, 400, 600 volts DC Working



Uninsulated Body Type CPM08



Insulated Body Type CPM09

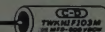
MILITARY & INDUSTRIAL

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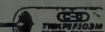
in accordance with

MIL-C-26244 (USAF)

200, 300, 400, 600 volts DC Working



Uninsulated Body Type TWKN
(equivalent to MIL-CPV08)



Insulated Body Type TWKP
(equivalent to MIL-CPV09)

CAPACITANCE:
001 mfd. to 1.0 mfd.

TEMPERATURE RANGE:
-55°C to +125°C.



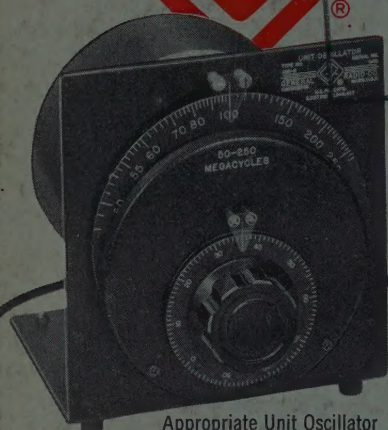
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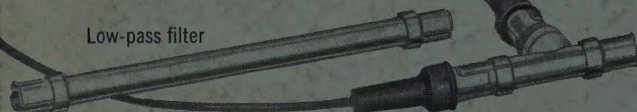


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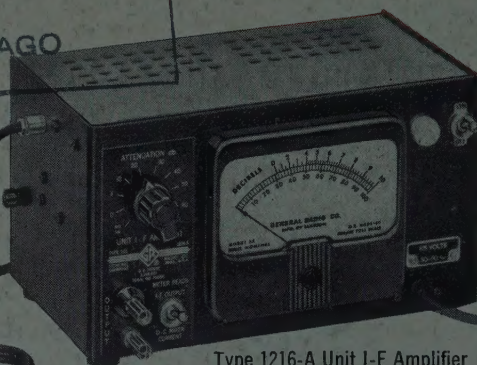
Appropriate Unit Oscillator



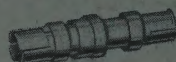
Type 874-MR Mixer Rectifier



Type 874-EL



Type 1216-A Unit I-F Amplifier
complete with oscillator power supply



Type 874-G10 10-db Pad

The DNT Detector Assembly operates on the heterodyne principle. Its local oscillator is set 30 Mc above or below the incoming signal to produce a difference frequency at the output of the mixer. Since the mixer operates linearly over an 80-db range, the level of the detected signal can be amplified and accurately measured with the calibrated step attenuator and meter built into the I-F Amplifier.

The **D**etector for High Frequency Measurements

USEFUL AS A

Bridge and
Slotted-Line
Null Detector

Detector for
Insertion-Loss and
Attenuation
Measurements

Detector for
Measuring Voltage Ratio

70-DB Step Attenuator Built In and a Meter Calibrated in DB for Interpolation Between Attenuator Steps — Mixer linearity over 80-db range permits direct measurement of levels. Calibrated attenuator has steps of 0, 3, 10, 20, 30, 40, 50, 60 and 70 db. Accuracy is $\pm(0.3 \text{ db} + 1\% \text{ of indicated attenuation})$.

AVC for Null Measurements — The I-F Amplifier can be switched to A-V-C operation, providing logarithmic instead of linear response. The AVC automatically increases sensitivity as balance is approached and prevents violent off-scale indications during unbalanced conditions.

High Sensitivity — The heterodyne principle of operation provides high, uniform sensitivity over wide frequency ranges. Four stages of amplification provide gain of 100 db. Less than $5\text{-}\mu\text{v}$ input from 50-ohm source will produce a 1% meter deflection over residual noise at any frequency between 50 and 950 Mc... less than $80 \mu\text{v}$ required for full scale deflection.

Broad Amplifier Bandwidth, yet Has Optimum Selectivity — System does not have to be retuned each time input signal drifts. Bandwidth between half-power points is 0.7 Mc; at 2 Mc from center frequency, response is down more than 20 db; 60-db down at 5 Mc.

Excellent Shielding Throughout — Input signal is confined to a separate, well-shielded mixer unit. Internal amplifier parts are shielded and isolated from each other by numerous filters to minimize leakage and regeneration.

Wide-Frequency Operation

Detector	Range*	Unit Oscillator Supplied	Price
DNT-1	40-530 Mc	1208-B	\$626
DNT-2	40-280 Mc	1215-B	\$606
DNT-3	220-950 Mc	1209-B	\$659
DNT-4	870-2030 Mc	1218-A	\$879

*Higher frequency operation to 5000 Mc by using oscillator harmonics. Any of these assemblies may be converted to another by using the appropriate local oscillator and filter for that range. Units making up the DNT Assembly can also be used singly for other measurements.

Write for Complete Information

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